

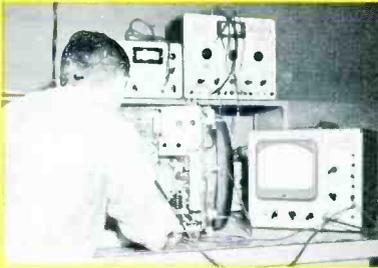
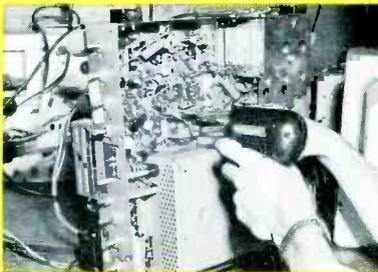
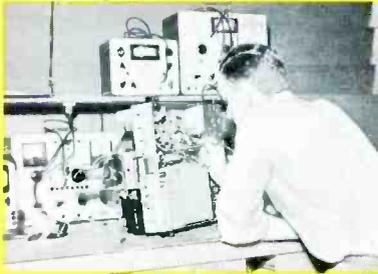
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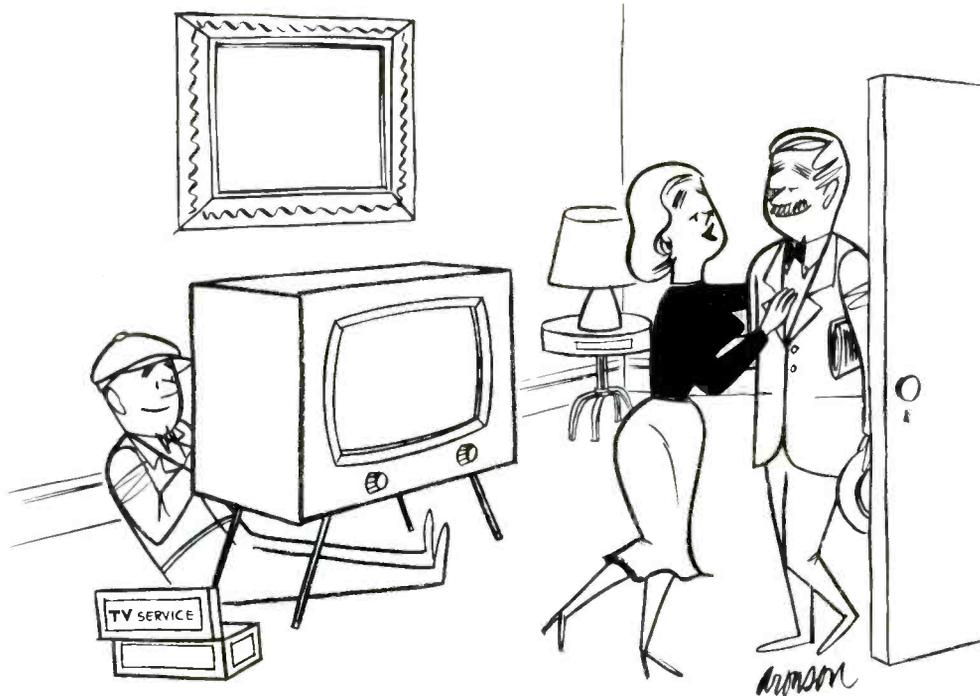
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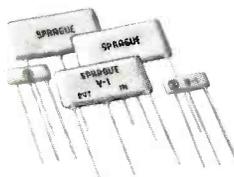
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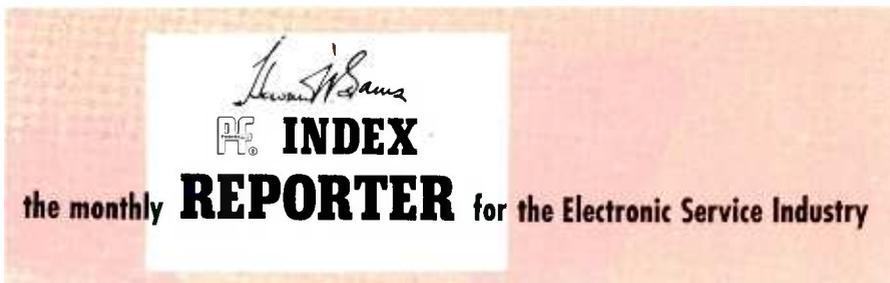
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CONTENTS

Shop Talk	Milton S. Kiver	5
Color TV Training Series (Part IV)	C. P. Oliphant and Verne M. Ray	7
Headsets for TV	Henry A. Carter	11
In the Interest of Quicker Servicing	Henry A. Carter and Calvin C. Young, Jr.	13
Notes on Test Equipment	Paul C. Smith	19
New Tubes for Series Strings	James M. Foy	21
Traps for Standard Coil Tuners	Don R. Howe	23
TV Colormath (Part V)	Harold E. Ennes	25
Horizontal AFC Circuits (Part IV)	William E. Burke	31
Audio Facts	Robert B. Dunham	33
Examining Design Features	Don R. Howe	37
Dollar and Sense Servicing	John Markus	39
+ More or Less —		96
Photofact Cumulative Index No. 46 Covering Photofact Sets—Nos. 1-251 Inclusive		97

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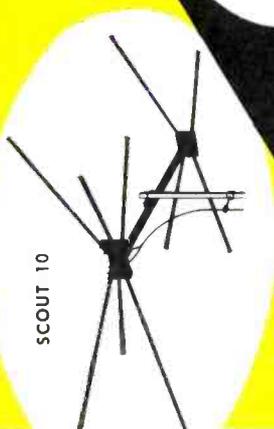
AUDIO	SERVICING
Capehart High-Fidelity Radio Phonograph Model RP-154 33	Bench Picture Tube 64 Headset Installations in TV Sets 11 RF Tuner Servicing 5 Sync Separators and Amplifiers 65 Traps for Standard Coil Tuners 23 TV Interference Problems 13
COLOR TV	TELEVISION
Bandpass Amplifier 25 Burst Separator and Amplifier 27 Color Killer 25 Color Picture Tube Circuits 51 Color Sync and Phase 41 Delay Lines 25 Hickok 655XC Color-Bar Generator 77 Matrix and Adder Circuits 47 RF Tuner Circuits 7 Sound IF and Audio Sections 59 Synchronous Demodulators 43 Video Detectors 9 Video IF Amplifiers 9	Arvin Chassis TE-340-1, -2 73 General Electric Model 21C240 37 Gruen AFC Circuit 31
	TEST EQUIPMENT
	Hickok 655XC Color-Bar Generator 77
	TUBES
	New Tubes for Series Strings 21

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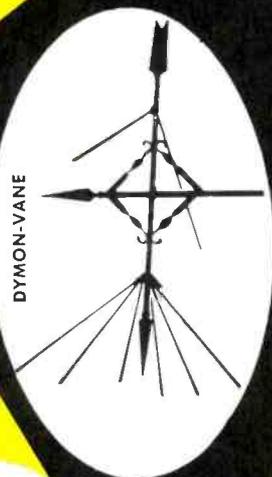
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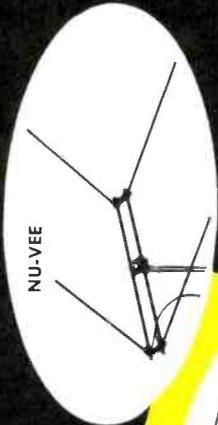
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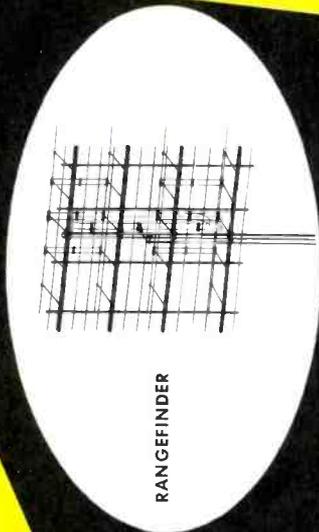
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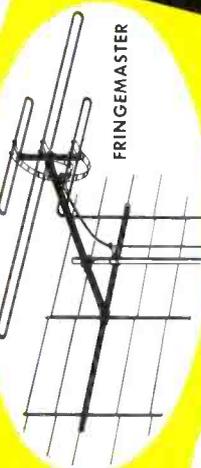
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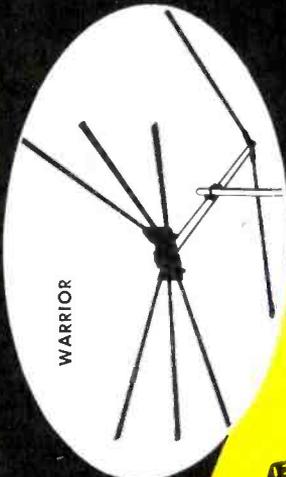
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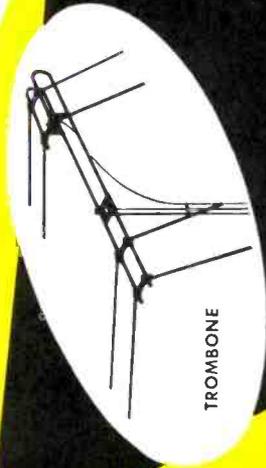
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ShopTalk

MILTON S. KIVER

President, Television Communications Institute

In last month's column, we discussed the electrical and mechanical troubles that a service technician encounters in his work on television tuners. Generally, the visual effect of one of these gross impairments is readily apparent to a trained observer, such as a service technician, so that he is quite aware that something is amiss.

There is, however, a more subtle difficulty that one encounters with tuners, and that is the problem of improving the sensitivity of a tuner which is already operating normally. This is frequently undertaken in weak-signal areas.

The sensitivity of a tuner, or its ability to amplify signals, is based upon three factors over which the service technician can exercise some form of control. These are: the AGC voltage, the RF amplifier tube, and the B+ voltage. Let us consider each in turn.

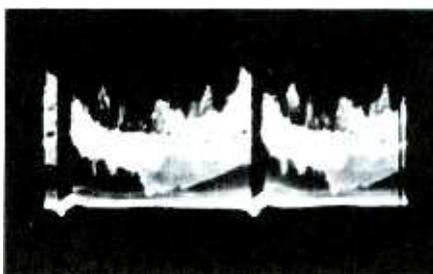
The AGC Voltage

The AGC voltage is designed to regulate the gain of a stage through the variation of grid bias. The more negative the bias, the lower the stage gain. Thus, to increase the gain, the AGC voltage should be made as low as possible; and this line of attack can be followed to increase the sensitivity of a tuner. Each step must be taken carefully, otherwise set reception may be harmed rather than helped.

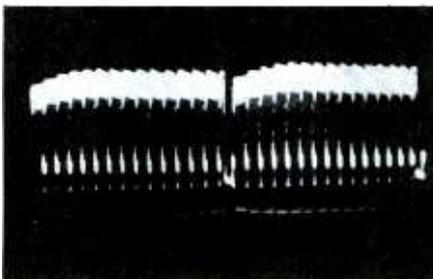
The following is one of the ways that has been found useful. Set up the receiver at the customer's location so that the signal strength there can be used during the adjustment. Connect an oscilloscope through a 10,000-ohm isolating resistor across the load resistor of the video detector. At the same time, connect the antenna

to the receiver and tune in a local station. The video signal should appear on the scope screen as well as on the picture tube screen. Slowly lower the AGC bias which is fed to the RF stage, and keep an eye on the video-signal pattern appearing on the scope screen. Be particularly watchful of the sync pulses to make certain that they are neither compressed nor eliminated altogether. See Fig. 1. If compression should occur, stop reducing the AGC voltage. On the other hand, if there is no signal compression or distortion even when the AGC voltage is reduced to zero, then it is safe to remove this voltage completely and operate the RF amplifier without it.

The foregoing procedure should be carried out with the set tuned to



(A) Sync Pulses Compressed.



(B) Sync Pulses Completely Removed.

Fig. 1. Video Signal Indicating Overloaded RF Amplifier.

the strongest signal it will receive. Suppose that you encounter a situation where there is one station which is noticeably stronger than the other or others; suppose you find that there are several stations, each with a considerably different level of input signal. What then?

The best solution is to tailor the operating bias separately to each signal, and this can be done by installing a small selector switch on the rear apron of the set. Then, for each selector position, a network can be installed which will bring the AGC bias for the RF stage to the desired level. The job is not particularly difficult to carry out, and it works rather well.

One word of caution: due to the vagaries of television reception, it is best not to lower the AGC bias to the exact point where sync pulse compression commences. Leave some leeway by maintaining the bias about 10 per cent above the critical value.

The next question is: "How do you go about reducing the AGC voltage applied to the RF amplifier?" This will vary to some extent with each different set, but a general method that has proved successful is to start with a 1-megohm resistor connected between the AGC line leading to the RF amplifier stage and ground. See Fig. 2. Then gradually lower the value of this resistor while watching the effect on the video signal appearing on the scope screen. Set the resistor value at the point where the signal amplitude is greatest without distortion.

In some circuits, there is no isolating resistor in the AGC line between the point where it leaves the IF system and where it enters the

* * Please turn to page 81 * *



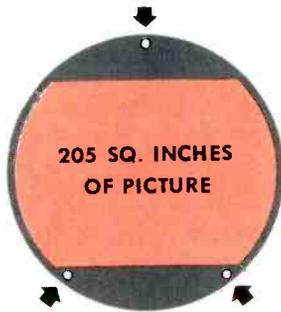
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COLOR TV TRAINING SERIES

PART IV COLOR RECEIVER CIRCUITS

by C. P. Oliphant and Verne M. Ray

Introduction

The preceding sections of this Color TV Training Series were devoted to studies of colorimetry, the development of the color television system, and the make-up of the color television signal. These subjects, together with a working knowledge of black-and-white receivers, are essential before attempting to understand the operation of color receiver circuits. The following material is intended to provide the reader with a fundamental knowledge of the way in which a color receiver operates.

The study of color receiver circuits has been divided into two categories. The first deals with the color receiver sections which are similar to those used in monochrome receivers. In this respect, the material presented deals mainly with the changes which have been made in these sections in order to achieve color reception. If a particular color receiver circuit is quite similar to its counterpart in the black-and-white receiver, very little discussion is given to it since the reader already has an understanding of its operation from his past experience with black-and-white television.

The second category has to do with color receiver sections that are specifically designed for the chrominance portions of the composite color signal. These circuits are not used in monochrome receivers; therefore, a detailed discussion of them will be presented. The discussions which follow resulted from examinations of color receivers made by several manufacturers. The circuits discussed are selected from individual receivers, and they are intended to serve as representative circuits which perform a given function. In some cases, two or more circuits which accomplish the same function are shown; but this is done only when different methods of operation or design are used.

Rapid developments in color television are being made; however, these developments will not change the basic function of a color receiver. Therefore, any knowledge obtained from this study will be a definite aid in understanding color television and can be applied to the new circuits which may be developed in the months to come.

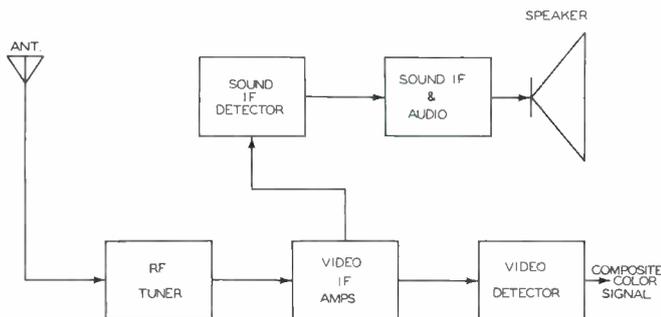


Fig. 4-1. Block Diagram of Color Receiver Sections Discussed in This Issue.

The sections to be discussed in this issue are shown by the block diagram of Fig. 4-1. It can be seen that this portion of a color receiver is not too much different from that of a monochrome receiver. With the exception of a block representing the sound detector, this drawing could represent the RF, IF, and sound circuits of any television receiver. Nevertheless, the following circuit discussions show some important differences.

RF Tuner

The function of the RF tuner in a color receiver is the same as in monochrome receivers, and the physical appearance of the unit is not changed; however, there is one requirement of the RF circuits in a color receiver

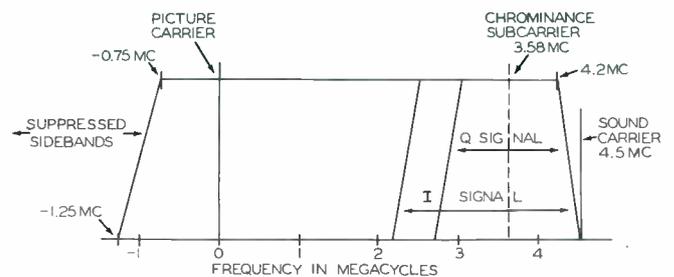


Fig. 4-2. Frequency Relationships of Color Television Signal Components.

that does not necessarily apply to monochrome operation. This concerns the allowable tolerance in the frequency response of the tuner.

It has been previously pointed out that a color television signal contains both luminance and chrominance information. As seen in Fig. 4-2, this information extends from 0.75 mc below to 4.2 mc above the picture carrier and falls to zero at 1.25 mc below and slightly less than 4.5 mc above. If a tuner designed for a black-and-white receiver were to be used in a color receiver, nonuniform amplification of all frequencies might result and cause poor color reception. Although a tilt or sag in the response of the RF tuner might be compensated for

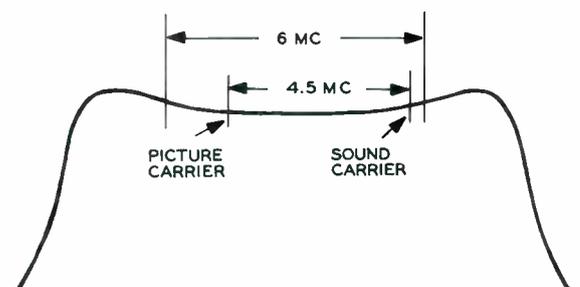


Fig. 4-3. Ideal Frequency Response of Tuner Used in Color Receiver.

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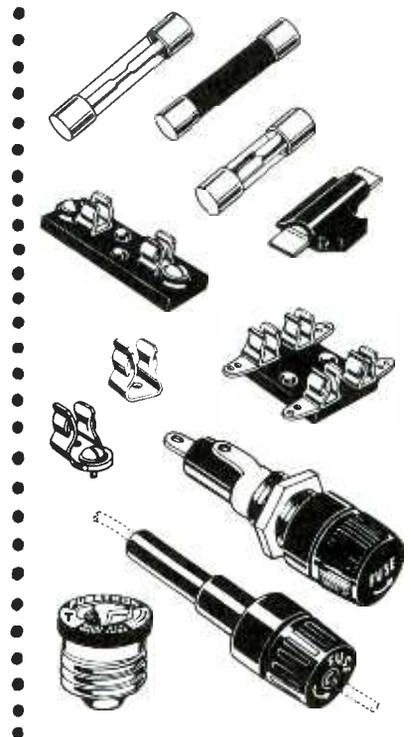
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in the IF amplifier section, it is necessary to provide uniform bandpass characteristics in the tuner in order to tune all channels properly. Fig. 4-3 shows the frequency-response curve of an RF circuit which would produce excellent results in a color receiver.

To illustrate the similarity of the circuitry in a tuner designed for a color receiver and that of a tuner designed for a monochrome receiver, a schematic of a Standard Coil tuner designed for color is shown in Fig. 4-4. Note that the circuit is very similar to Standard Coil tuners currently being used in black-and-white receivers. There is one feature, however, which warrants special note. It can be seen in the circuit drawing that the secondaries of the antenna coils for the lower channels 2 through 6 are tuned with iron-core slugs. This is done to make possible the adjustment of these coils at the lower frequencies. At the lower channels, the Q of the circuit is higher; therefore, the bandpass is narrower and the coils require adjustment to achieve flatness in the response curve over a 6-mc range.

Past experience has shown that RF tuners in monochrome receivers are quite stable and present only a moderate number of servicing problems. Tuners in color receivers will undoubtedly present additional servicing problems because they must operate more precisely than those in a monochrome receiver. A defectively operating tuner in a monochrome receiver might not be suspected, but one that is operating in a similar manner in a color receiver might result in faulty operation of the color circuits. Such a condition would obviously result in a complaint. When the tuner in a color receiver is being serviced, particularly during alignment, the requirement of the tuner must be kept in mind. Many of the compromises which are in common practice in servicing monochrome receivers cannot be made in color work.

Video IF Amplifiers and Video Detector

Although the requirements of the video IF section are more specific in a color receiver, the function is essentially the same as in monochrome receivers. Before examining the circuit design, let us consider what is required of the video IF section.

First of all, the purpose of the section is to provide amplification and selectivity to a band of frequencies. This band should extend from .75 mc below to around 4.2 mc above the picture-carrier IF in order to include all of the luminance and chrominance information. Four or five stages are needed for this function ordinarily. The video IF strip should also severely attenuate the sound IF carrier, more so than in monochrome receivers. The reasons for this will be given later in this discussion.

A curve illustrative of good over-all frequency response through the RF and IF sections of a color receiver can be seen in Fig. 4-5A. Compare this curve to the one in Fig. 4-5B which is representative of the overall frequency response of later model monochrome receivers. It can be particularly noted that the response of the color receiver is very critical in the region of the sound carrier where the slope of the curve is very steep. Frequencies only .35 mc away from the maximum attenuation point at the sound-carrier frequency are provided with at least 90-per-cent amplification. The reason for this is that the upper sidebands of the chrominance subcarrier extend to this portion of the frequency curve. To illustrate this, the frequency limits of the color picture signal have been superimposed on the response curve of Fig. 4-5A. Although the response curve in Fig. 4-5B would produce good results on a monochrome transmission, it would severely attenuate the chrominance information contained in a color transmission. This loss of chrominance would result in poor color reproduction or complete loss of color reception.

The video detector is required to remove the luminance, chrominance, and sync signals which constitute the composite color signal. A crystal diode with an IF filter is commonly used. The video detector in a color receiver differs from that in a monochrome set by having usually a 41.25-mc sound-carrier trap in its input. This trap insures against the development of 920 kc, which is an undesirable beat between the sound carrier and the frequency representative of the color subcarrier. The sound take-off point is located ahead of this trap.

* * Please turn to page 55 * *

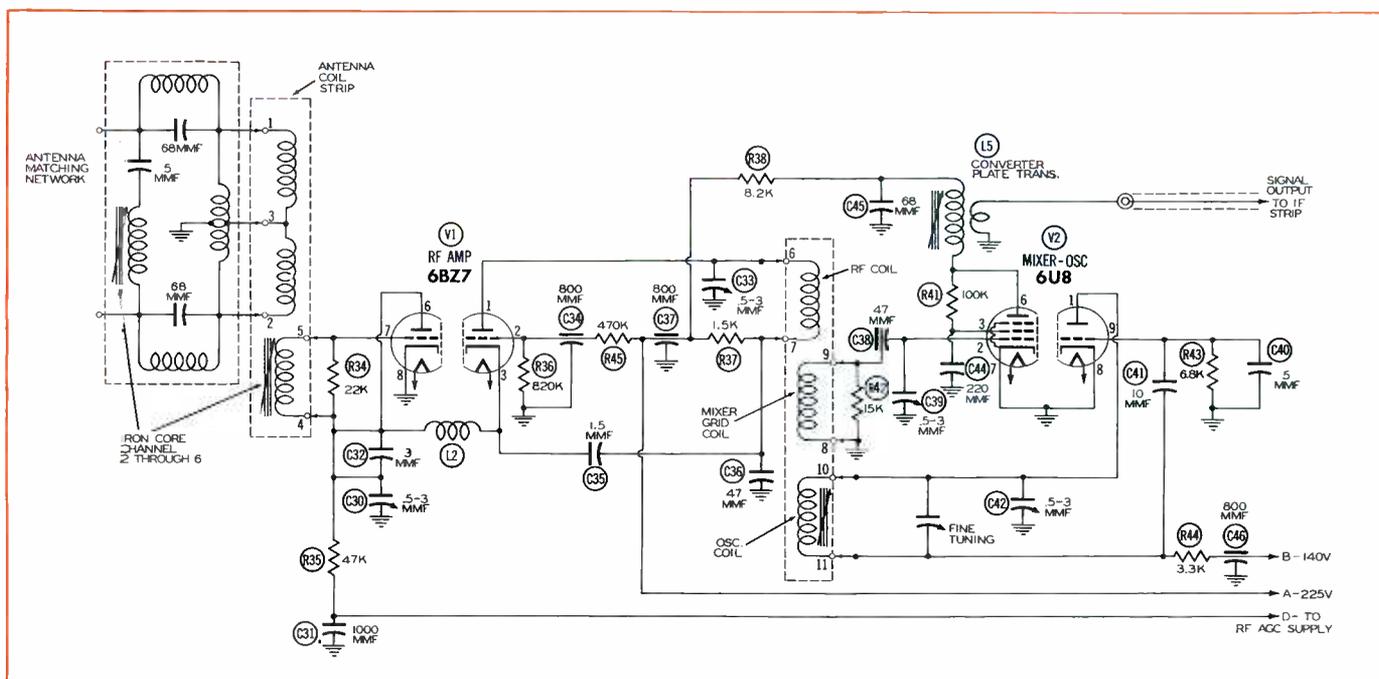


Fig. 4-4. Standard Coil Tuner Used in Westinghouse Model H840CK15 Color Receiver.



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Simple and Elaborate Circuits for Connecting Headsets

There are two primary reasons why set owners might want headsets connected to their TV receivers. The reason most often given is privacy of hearing. One person may want to watch a program while another is reading or sleeping in the same room and does not want to be disturbed by the sound from the receiver. Parents quite often desire headsets on their television receivers so that they can entertain guests at a game of bridge or the like while their children are watching and enjoying a program.

The other reason for using headsets is based upon the fact that sound is much more enjoyable to those with impaired hearing if the sound is heard directly from the receiver through the use of headsets than if the output of the speaker is reamplified by a hearing aid. The matter of acoustics and other factors that make this true will not be considered at this time.

Of these two chief reasons for desiring headsets, the use by persons with impaired hearing is the one which will require the most consideration and care in setting up satisfactory equipment. The reason for this should be quite clear. In the first place, it is almost imperative that the headset have some means whereby the volume can be adjusted to suit the hearing ability of the wearer. In addition to the volume control, it may also be advantageous to provide a means for the wearer to control the tone range of the headset.

HEADSETS for



TV

by Henry A. Carter

Hookup—Should It Be Simple Or Elaborate?

There are many ways in which a pair of earphones or a headset can be connected to a TV receiver. The circuitry may be simple or quite complex, depending upon the quality of performance that the set owner desires. Many things must be considered. For instance, is the headset to be used for privacy of hearing, or is it for a partially deaf person? Is it for use in a hospital room, so that the sound will not disturb other patients, or in a noisy room, so that the headphones will shut out distracting noises? The type of hookup also depends upon the circuit of the receiver. Is the receiver an AC-DC type, or is it one of those types of sets having one side of the AC line and one side of the speaker connected to the chassis? In either of these types,

there is great danger of a shock to the person who wears a headset that is improperly installed. Any chance contact with a defective electrical appliance is likely to result in a shock to the user of such equipment. This fact should be kept in mind when choosing the particular circuitry for the headset.

We must also consider the need for controlling the volume of the headset separately from that of the receiver when speaker and headset are to be used simultaneously. After all, a headset is not matched to a speaker to produce equivalent volume with the same signal applied. Therefore, a separate volume control is almost a necessity in these cases.

Generally speaking, the greater the performance requirements specified by the set owner, the more elaborate the headset installation must be. Naturally the cost of such an installation becomes greater also. Safety should be a primary consideration regardless of the type of hookup employed.

Types of Hookups

Of all the possible hookups, the method which has the most advantages is one which employs a separate audio-output tube for driving only the headsets. Fig. 1 shows a typical circuit of this type. This circuit has at least four distinct advantages over the more simple hookups.

First and foremost of these advantages is the fact that this circuit

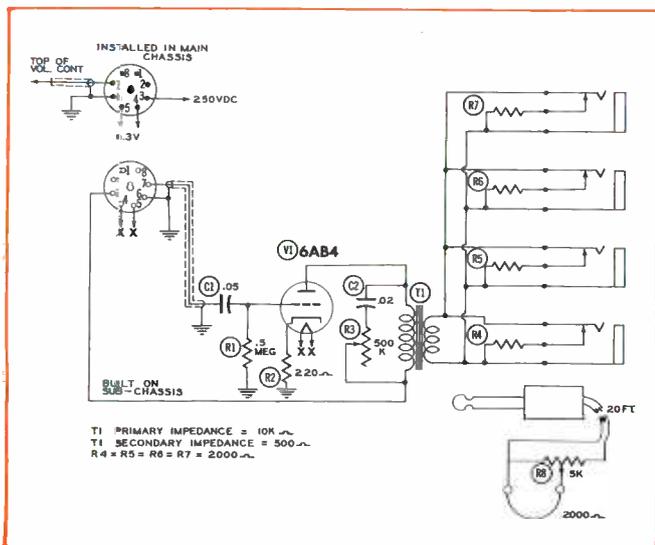


Fig. 1. A Method of Connecting Several Headsets to One TV Receiver Without Affecting Speaker Operation.

* * Please turn to page 51 * *

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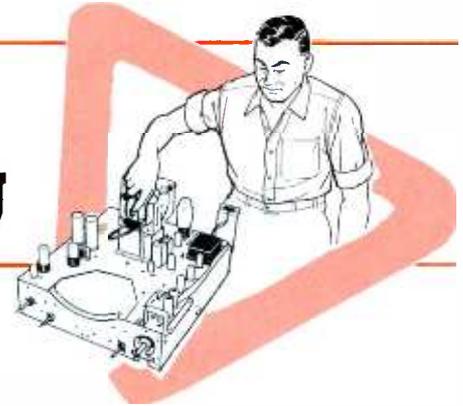


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Quicker Servicing

by Henry A. Carter and Calvin C. Young, Jr.



IN THE HOME

Effective correction of the many kinds of television interference is one of the more difficult problems encountered by the television technician during a home service call. These interference signals, although appearing in many different forms, actually may be placed in two major categories:

1. Signals generated within the television receiver in question.
2. Signals generated externally.

The interference signals generated within the receiver are usually caused by improper tuning, poor alignment, unsatisfactory shielding, or the failure or change in value of some component. Some of the internally generated interference signals encountered more often are as follows:

1. A 4.5-mc beat in the picture.
2. Bars due to horizontal-sweep radiations feeding into the video.
3. Tunable ghosts due to video IF regeneration.

4. Barkhausen oscillations.

The interference signals which are externally generated take on many different forms and have a variety of origins. A list of those more often encountered is as follows:

1. Interference from another TV station.
2. Ignition interference.
3. Interference from amateur radio equipment.
4. Interference from electric motors, lights, and other electrical appliances.
5. Ghosts due to signal reflections.
6. Local-oscillator interference from another TV receiver.
7. Interference from diathermy or industrial heating apparatus.

Figs. 1 through 4 are illustrations of the effects of interference from external sources on a transmitted test pattern or picture. The discussion which follows gives the

characteristics of these interferences and the possible means of eliminating or minimizing them.

Fig. 1 is an illustration of the interference pattern produced by 4.5 mc. This pattern is usually caused by a slight detuning of the receiver or a misalignment of the 4.5-mc trap. A characteristic of a 4.5-mc beat due to receiver trouble is that the beat can be minimized by adjusting the fine-tuning control. In most cases, readjustment of the 4.5-mc trap and the receiver fine tuning will correct this trouble.

Fig. 2 is an illustration of the pattern produced by a 15,750-cps radiation being picked up from the horizontal-sweep section by the video amplifier. This trouble is usually due to improper lead dress in the video amplifier stage, to improper lead dress in the input circuit of the picture tube, or to improper shielding of the horizontal-output and high-voltage sections. Correct installations of the high-voltage cage assembly and proper lead dress of the lead to the driven element of the picture tube will in most cases eliminate this trouble.

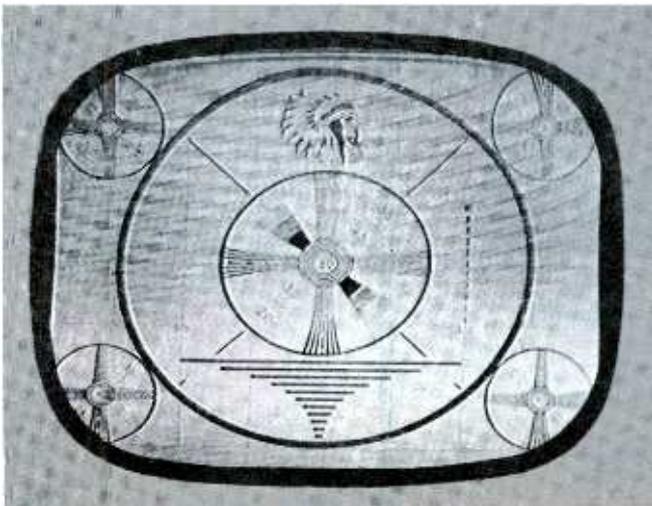


Fig. 1. A 4.5-Mc Beat Pattern.

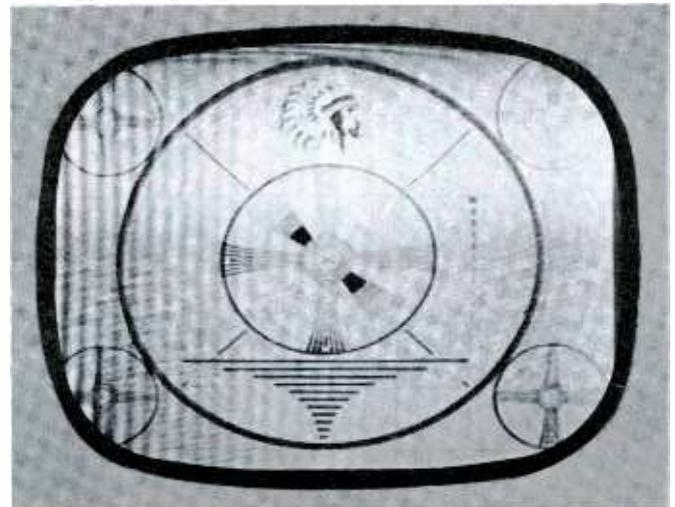


Fig. 2. A 15,750-CPS Beat Pattern.

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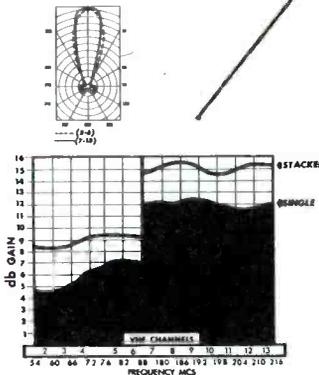
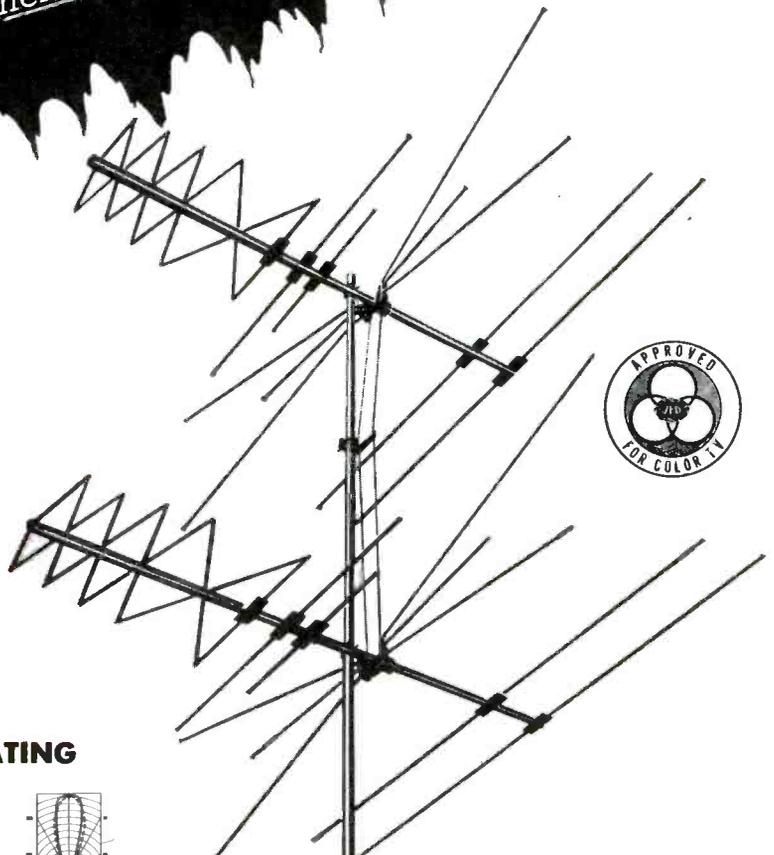
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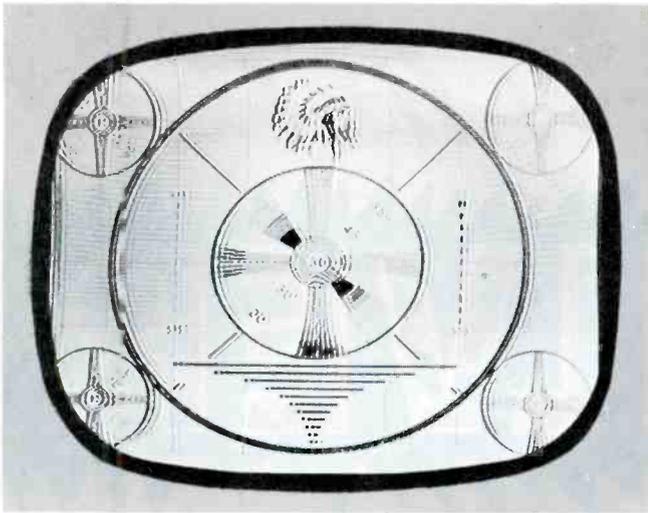


Fig. 3. Tunable Ghosts Due to Video IF Regeneration.

Fig. 3 is an illustration of tunable ghosts due to regeneration in the video IF strip. The major characteristics of this type of interference are: (1) spacing between ghosts will vary with setting of the fine-tuning control, (2) shading will vary with setting of the fine-tuning control, (3) reversing of the contrast may occur with setting of the fine-tuning control. This type of interference is usually caused by a faulty tube in the video IF stages, a faulty bypass capacitor in the video IF strip, or poor alignment of the RF or IF section of the receiver.

Fig. 4 is an illustration of Barkhausen oscillation. This type of interference is a spurious oscillation generated in the horizontal-output stage and is characterized by one or more black vertical lines in the left portion of the picture. The interference is most noticeable on weak signals where receiver gain is at or near maximum. Readjusting the horizontal-drive control or replacement

of the horizontal-output tube will in most cases correct this trouble. In some extreme cases, it has been necessary to replace the horizontal-output or flyback transformer. Poor connections on the plate cap leads of the horizontal-output tube and high-voltage rectifier tubes may also cause this trouble.

Some of the externally generated interference signals which are frequently encountered are illustrated in Figs. 5 through 13. A discussion of the characteristics of the possible cures for each type of interference is presented in the following paragraphs.

Fig. 5 is an illustration of interference from another television station transmitting on the same channel. This type of trouble is usually found in areas between two television stations operating on the same frequency where the signal strength from either is sufficient to obtain a picture. The installation of a highly directional antenna with a high front-

to-back ratio should correct this trouble.

Fig. 6 is an illustration of ignition interference. This type of interference is most noticeable in weak-signal areas. The effect of this type of interference may be minimized by relocating the antenna away from the street or highway and rerouting the antenna lead-in wire to the side of the house away from the traffic. In some cases, using shielded lead-in wire will also help. There are available filters which are said to eliminate ignition interference. The black specks in the picture, incidentally, are the ignition pulses; and the white specks are interruptions of the horizontal-scanning line.

Fig. 7 is an illustration of interference from amateur radio equipment. The frequency of the interfering signal is approximately 28 mc. This type of interference can in most cases

* * Please turn to page 63 * *



Fig. 4. Barkhausen Oscillations.

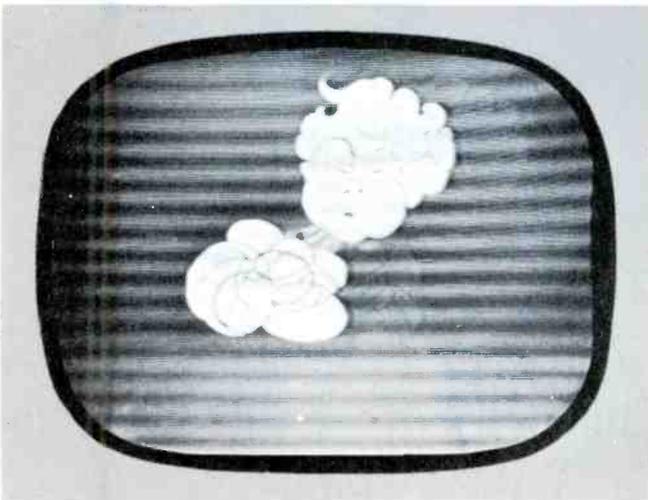


Fig. 5. Cochannel Interference.

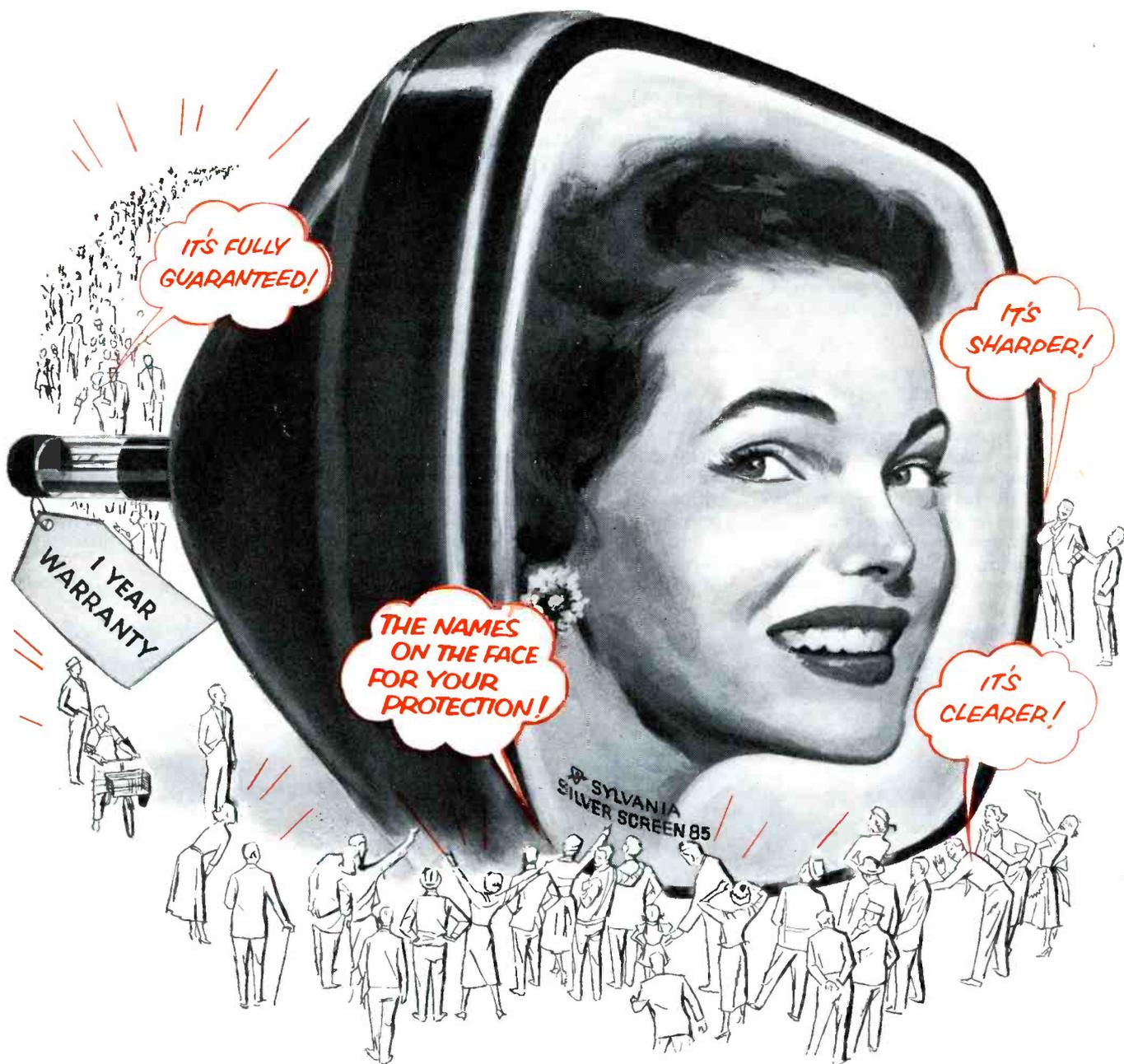


Fig. 6. Ignition Interference.

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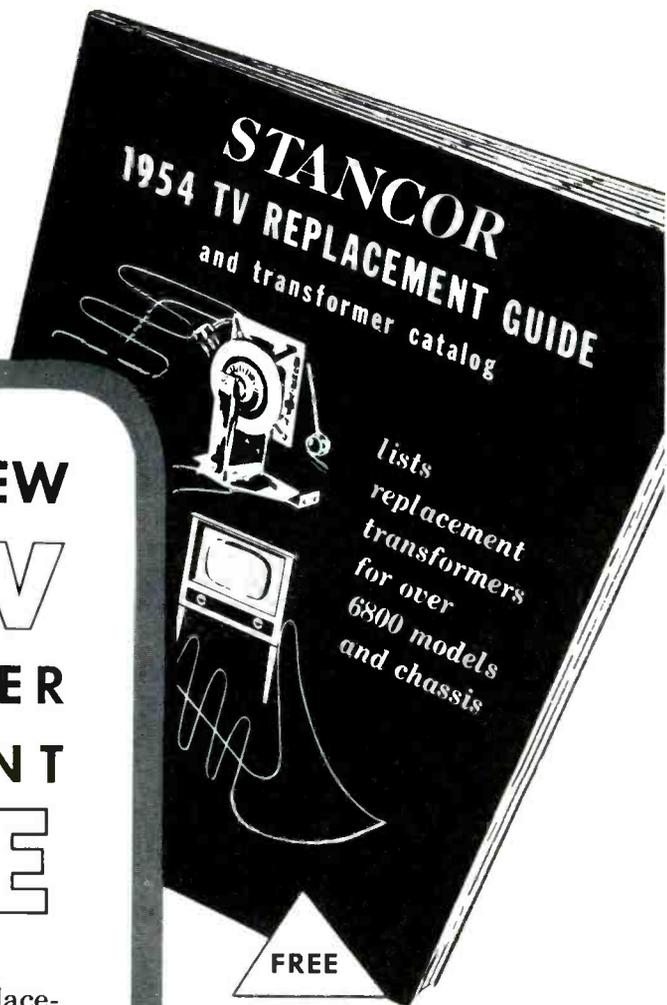


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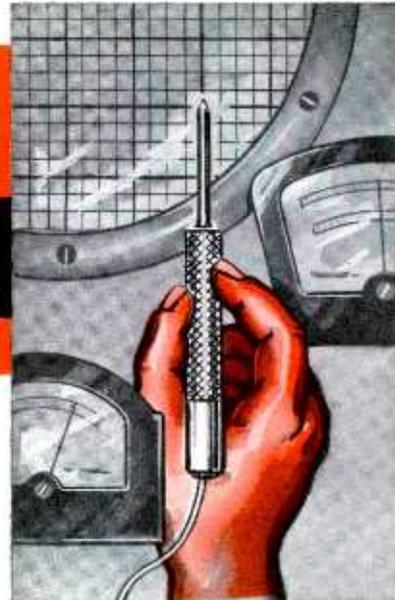
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Notes On

TEST EQUIPMENT

Presenting Information on Application, Maintenance, and Adaptability of Service Instruments



by Paul C. Smith

Test-instrument manufacturers are very prompt in meeting the needs of the service technician as new developments arise in the fields of monochrome and color television. The result is that almost before a new device is in the hands of the public, instruments for its proper adjustment and servicing are available for the service technician. So he is not subjected to the frustration of an unsuccessful search for proper test instruments — rather, he is faced with the alternate problem of making the best choice of instruments to suit his needs from the array which is set before him.

This choice will be influenced by a number of factors, not the least of which is cost. The latter item may be anything from under \$50 for a good multimeter to over \$300 or \$400 for a sweep generator, a color-bar generator, or an oscilloscope. At first glance this looks like a considerable outlay of money for instruments, especially when a technician is just starting up in business and must obtain a complete line of equipment. When the cost of an instrument is rated over a period of time corresponding to its useful life, the picture does not appear so discouraging. For example, if we figure that a \$300 instrument will be used for a period of about six years (and many are still operating satisfactorily for a longer period than that), then the service technician is paying approximately one dollar a week for the use of the instrument during that time.

It should also be considered that the purchase of equipment can be viewed as a form of operating expense as much as rent and utilities; in fact,

it is good business to prorate such expense over a period and include it when calculating rates for servicing charges. In locations where regulations permit, a certain percentage of equipment cost may also be taken as depreciation for tax-calculation purposes; and naturally, the equipment owner will wish to avail himself of this privilege where it is extended. This privilege makes the picture even less discouraging in regard to the original heavy investment.

Several questions which naturally occur both to the beginning technician and to the seasoned veteran are these: How much test equipment is needed? What is the minimum equipment necessary to do the job efficiently and profitably? Generally, how long should test equipment be expected to last?

The answer to some of these questions will depend to a great extent upon the natural ability or the acquired skill of the service technician himself. Some who are able to utilize instruments to their fullest possibilities because of a complete understanding of the theory of their operation can perform a satisfactory service job with the minimum of test instruments. At the same time, these same technicians are the ones who benefit most from the addition of new equipment. We believe that it is not possible for technicians to know too much about the theory of operation of their instruments. The time spent in learning the use of a new piece of equipment is not lost; the principles involved are electronic, just as with the electronic devices that are brought in for servicing; and any knowledge picked up by a study of

test-instrument operation may prove useful in solving servicing problems.

A technician should be so familiar with his test equipment that its use becomes second nature to him much as an expert driver pilots his automobile through thickest traffic without conscious effort. Such expertness is not acquired overnight in either case.

The minimum test equipment required will depend not only upon the ability of the user but upon the service to be performed. If a technician services only radios (and some still do), he can get by with very little equipment. For servicing TV receivers he must add a few more instruments, and for color receivers he needs still more. The following would probably be the minimum for servicing a color receiver: a VTVM, a sweep generator, a crystal-controlled marker generator, a wide-band oscilloscope, and a color-bar generator. A white-dot generator would prove extremely useful, also. We are not recommending that the technician limit himself to these; but they are probably the absolute minimum necessary to perform satisfactory color TV servicing.

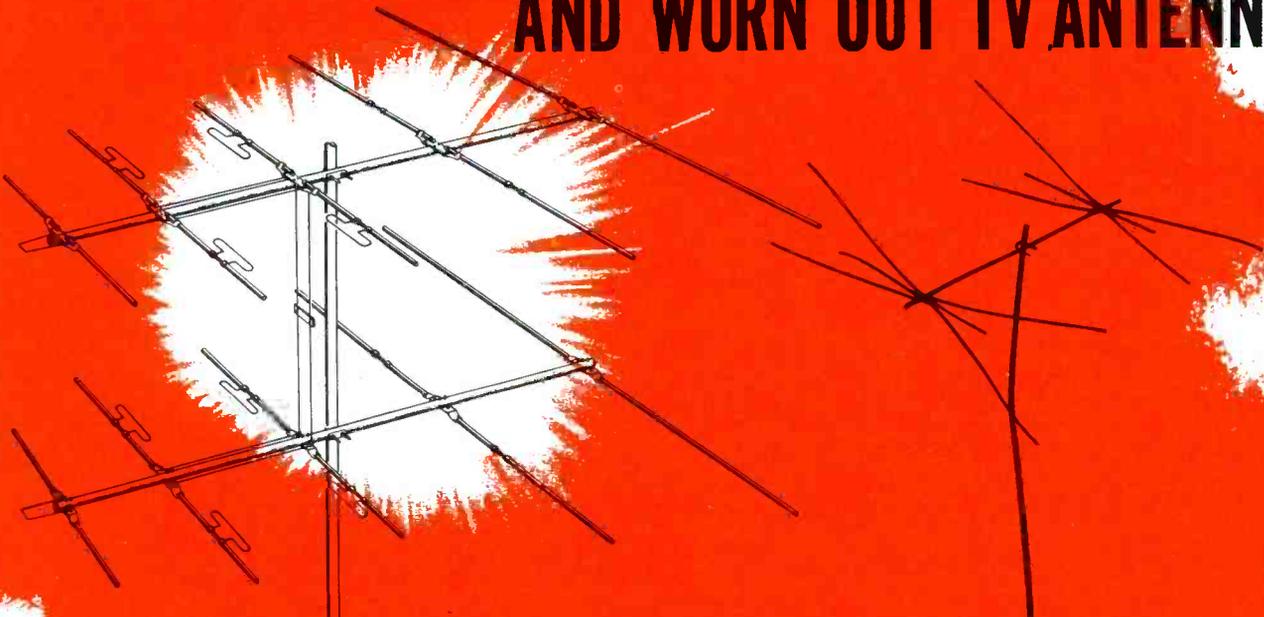
Over a period of use, there will be a certain percentage of failures among test instruments. Most of these will probably be normal tube failures: capacitor leakage or opens, resistance changes, and the like. Test leads will become frayed or broken with usage. Many repairs can be ef-

* * Please turn to page 76 * *

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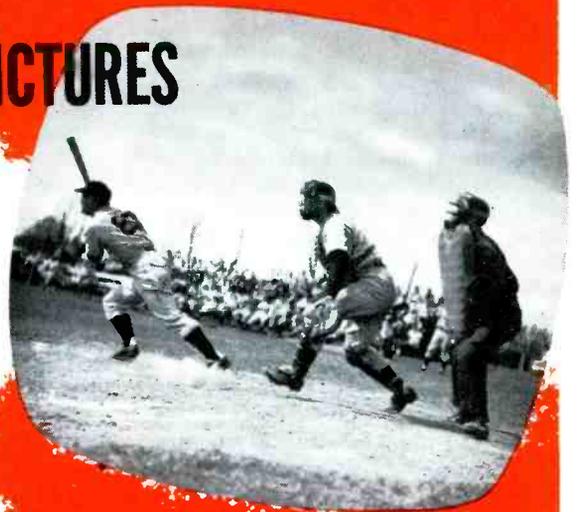
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NEW TUBES for Series Strings

by JAMES M. FOY

Minimizing Voltage Surges and Tube Burn-Outs in Series-Connected Filaments

The vacuum tube is the unit around which practically all of our electronic circuits are built. By exercising control of electron flow, tubes can be made to produce oscillations and to rectify and amplify voltages; in fact, the tasks they perform are so many and so varied as to be almost innumerable.

The design and manufacture of these tubes is an exact science, with the manufacturer constantly striving to meet current requirements. Any attempt to cover all the phases of this complex business in one short article would be next to impossible. Therefore, we will confine ourselves to only one of the problems with which the tube industry has been confronted. This problem has to do with the voltage surges and tube burn-outs in series-connected filament strings. Tube manufacturers have been working on this problem, and new tubes have been recently developed in an effort toward a solution.

For reasons of cost, ease of construction, weight, and other such practical factors, set manufacturers would prefer to use series-filament circuits instead of parallel-connected filaments which require transformer windings as voltage sources. The disadvantage of series-string operation has been that surges of current and voltage occur in the filaments of some of the tubes in the circuit. These surges momentarily increase the filament temperature and materially reduce the tube life.

Series Operation

To raise the temperature of a directly or indirectly heated cathode, power must be dissipated. This power should be enough to produce the

desired rate of emission in the cathode, and tube heaters are designed to meet this requirement. When excessive power is dissipated, the usable life of the heater and cathode in the tube is shortened.

If a transformer winding furnishes voltage to heat the filaments and the tubes are connected in parallel, no particular difficulty is presented since the transformer voltage is the same as the rated heater voltage. The correct voltage and therefore the correct power is available to the tubes at all times. This

does not hold true when the filaments of a number of tubes are connected in series.

In a series string, there may be surges of voltage across some of the tubes in the circuit. These surges are directly related to the fact that a difference exists in the initial or cold resistance and the final or hot resistance of a tube filament. The results of a variation of hot and cold resistances can be seen if we apply Ohm's law. For the purpose of illustration, let us consider two tubes with their filaments connected in series. The filament in each tube is rated at 6.3 volts and 300 milliamperes. If 12.6 volts are applied to these tubes and if a 300-milliampere current flows after they warm up, the hot resistance ($R_1 + R_2$) of the two tubes in series can be computed as:

$$R_1 + R_2 = \frac{12.6}{.300} = 42 \text{ ohms.}$$

Moreover, if the voltage drop across each tube is the same, the hot resistance of each filament is equal to 21 ohms.

Let us now consider what happens when these same tubes are cold. We know that the cold resistance of a filament is less than its hot resistance; however, the value of the cold resistance may vary from tube to tube. The warm-up time will also vary in different tubes. Fig. 1A shows the voltage, current and power values which exist at the instant of voltage application to the series string. The cold resistance of tube V1 is 9 ohms, and that of tube V2 is 7 ohms. By Ohm's law the values of voltage, current, and power can be computed; and they are listed in the illustration.

* * Please turn to page 93 * *

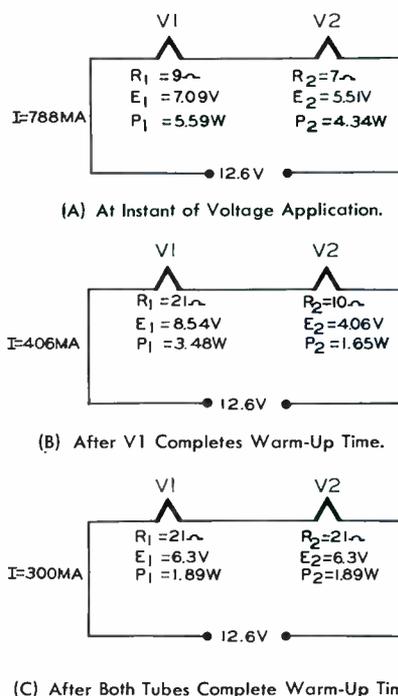


Fig. 1. Voltage, Current, and Power in a Two-Tube Series String During Warm-Up Period.

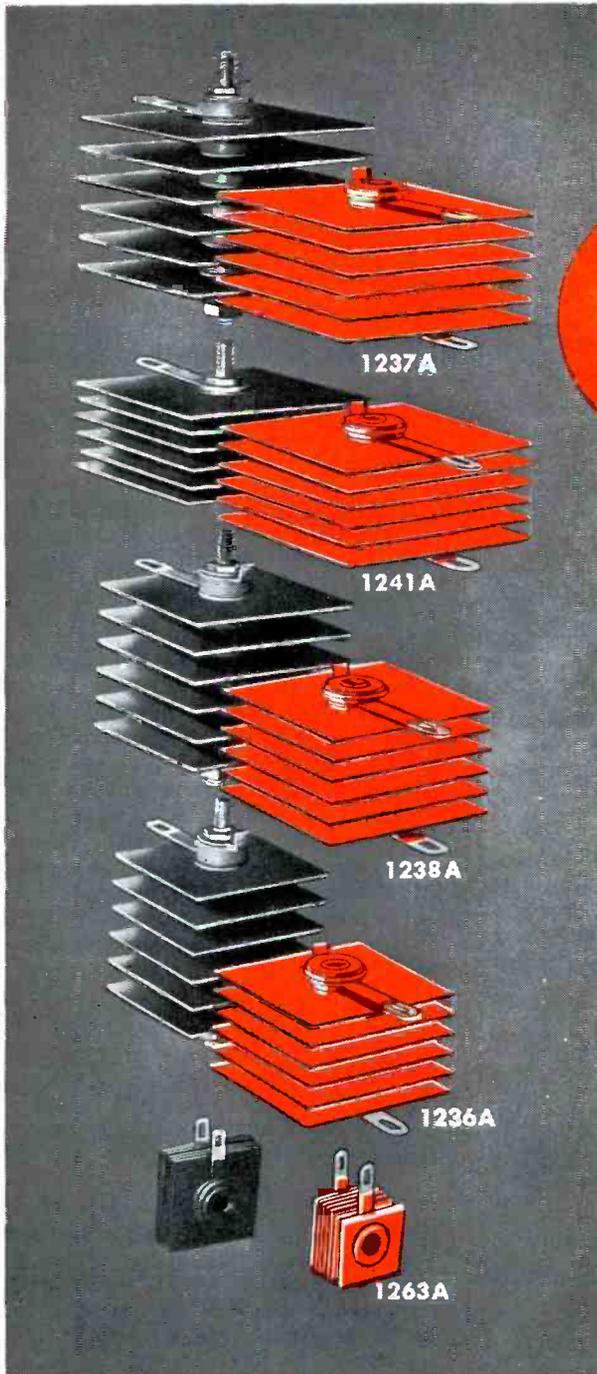
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1238A	350	1-3/8"±1/32"	1-3/4" Sq.
1241A	400	1-1/4"±1/32"	2" Sq.
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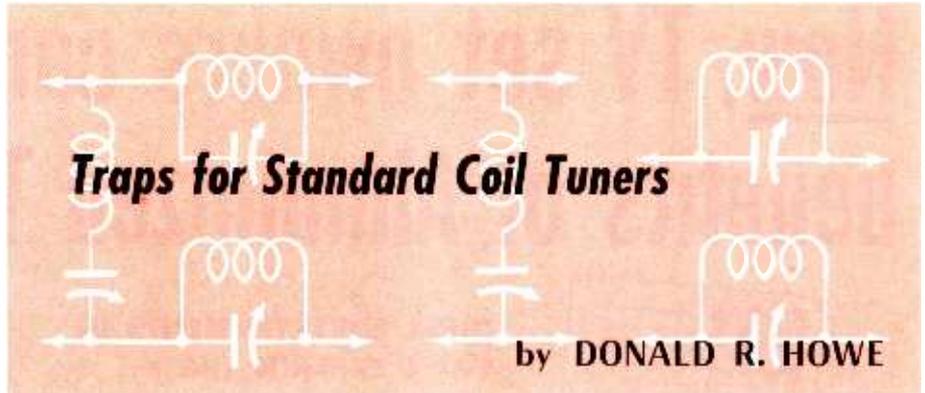
A Method of Eliminating Interference of Specific Channels

Continual improvement in the tubes and circuit designs employed in RF amplifiers has resulted in increased sensitivity for television receivers. This increased sensitivity together with the growing number of stations coming on the air has given rise to new problems in television interference. In order to alleviate these problems, manufacturers have incorporated in their receivers features that are consistent with good design practices. Among these features are high-pass filters and various forms of traps. In spite of these devices, interference problems continue to arise. A great number of these problems are the result of RF interference at a frequency of one of the channels. The interfering signal may be a harmonic from a transmitter, a beat between two transmitted signals, a signal on an adjacent channel, or the like. In this article, we are concerned with this type of signal that lies within the television band.

Upon consideration of the characteristics of this kind of interference, a trap would seem to be a logical solution to the problem. The reason for this conclusion can be shown by reviewing the action of a trap.

Traps are usually composed of inductance-capacitance (LC) circuits which are resonant at the frequency of the interfering signal. These LC circuits may be either series or parallel resonant, depending upon the manner in which they are used. The operation of a trap is based upon a fundamental principle of resonant circuits. A parallel-resonant circuit will offer a high impedance to a signal at the resonant frequency. The selectivity, or sharpness of response, of the resonant circuit is a function of the Q of the circuit. A very sharp response curve is characterized by a circuit possessing a high Q.

A series-resonant circuit offers a low-impedance path at the resonant frequency. The Q of this circuit will also affect the response. A series trap inserted across the antenna terminals of a receiver, as shown in Fig. 1A, causes a vertical short circuit at the frequency to which the trap is tuned. Signals at other frequencies are passed with very little loss. This



series trap becomes a simple but very effective way to eliminate undesired signals.

A series trap may also be placed between each antenna terminal and ground. Refer to Fig. 1B. When properly tuned, these traps will shunt the interfering signal to ground. At the same time, the traps provide a high impedance to ground for signals at frequencies other than at the resonant point.

An alternative to this method is to insert a parallel trap in each leg of the transmission line. This system offers a high impedance at the resonant point and results in a rejection of the interfering signal. This arrangement is shown in Fig. 1C.

In cases where the interfering signal is strong when compared to the desired signal, a combination of series and parallel traps may be necessary. An arrangement similar to the one shown in Fig. 1D can be used.

When traps are used to eliminate interference on one specific channel, it is quite possible that they will result in degraded performance on some of the other channels. It then becomes

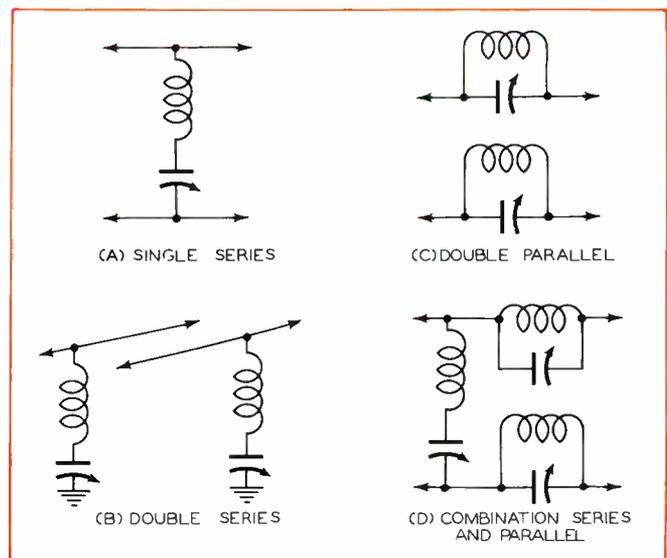
necessary to employ a method of removing the trap from the circuit when the trap is not required. This is ordinarily accomplished by installing an auxiliary switch on the receiver. The trap may then be switched in or out of the circuit as required. This may become annoying to the viewer, particularly if the channels are changed frequently; therefore, it would be extremely beneficial if a system could be devised to eliminate the auxiliary switch.

Another point to be considered is the proximity of the trap to the tuner input. The length of the transmission line from the trap to the tuner should be as short as possible. This is done to minimize the interference picked up in the line between the trap and the tuner. When the trap is placed close to the tuner, the trap will produce its maximum effect.

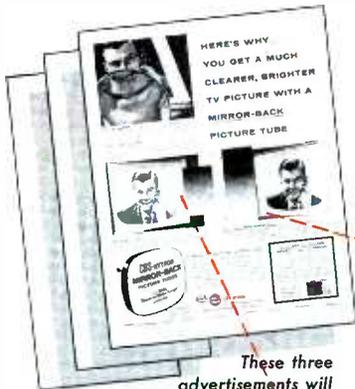
In many instances, a single series-resonant trap will be sufficient to remove the interference. If this is true, a very novel method may be employed to eliminate the extra switch, provided that a Standard Coil tuner is used in the receiver.

* * Please turn to page 74 * *

Fig. 1. Various Types of Traps.



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PART V

TYPICAL CIRCUITS AND COLOR FAULTS

Let us examine in detail typical color receiver circuits that differ from those used in the conventional monochrome receiver. It will be pertinent during the discussions to point out on a theoretical level the effects that circuit faults have on the results obtained in reproducing color images.

Delay Lines

A defective delay line is ordinarily replaced as an entire unit. It is important, however, to point out the importance of terminal impedances.

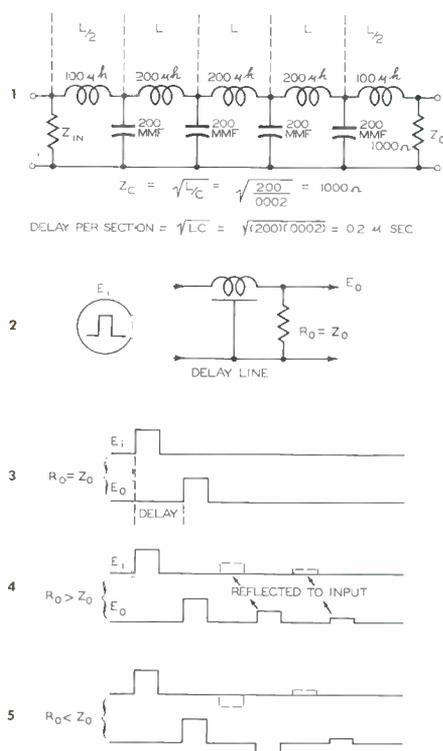


Fig. 14A. Typical Delay Line As Used in the Luminance Channel. Waveforms Illustrate the Effect of Proper and Improper Termination.

Fig. 14A, section 1, shows the schematic and characteristics of one type of delay line that is used in the luminance channel. The value shown for the amount of delay per section was calculated without taking into account any effects of mutual coupling. Since some mutual coupling exists in practice, the delay is usually somewhat greater than calculated from the square root of LC. Attenuation is negligible when the line is properly terminated in its characteristic impedance Z_0 .

With proper termination of the delay line as shown in Fig. 14A, section 2, an input pulse will appear in the output as a delayed pulse of practically the same amplitude. This action is illustrated in section 3 of Fig. 14A. In this case, all the energy is properly absorbed in the characteristic impedance constituting the delay-line load. When not properly terminated, energy is reflected back and forth between terminal points.

When the terminating impedance is higher than the characteristic impedance, spurious-pulse trains occur at an amplitude that depends upon the degree of mismatch. For an open circuit, amplitudes are reduced only in time by line attenuation and input resistance. For resistive termination of a finite value higher than Z_0 , spurious pulses are attenuated on each reflection. Fig. 14A, section 4, illustrates this action.

When the terminal impedance is less than Z_0 , reflections are inverted in polarity and attenuated by an amount determined by the low-load resistance. Section 5 of Fig. 14A illustrates this polarity reversal. Obviously, a short circuit would kill reflections and the entire signal.

The Mathematical Foundations Upon Which the Color TV System Operates

When the termination of the line is correctly loaded, the input resistance is unimportant except for gain considerations for the amplifiers concerned, since no reflections can occur. When the line is not properly loaded, the input resistance influences the amount and polarity of the signal reflections.

Fig. 14B is a partial schematic of a typical receiver and illustrates terminations and associated circuits of the delay line.

Bandpass Amplifier and Color Killer

Fig. 14C shows the first stage of the chroma section. R2 of the chroma input is ganged as a second section of R1 of the luminance input. R1 and R2 make up the over-all picture-contrast control. Since the proper ratios of Y-channel gain to chroma-channel gain must be maintained throughout the system, these controls operate together. Proper balance of respective channel gains may then be adjusted by individual gain controls later in the chroma channels.

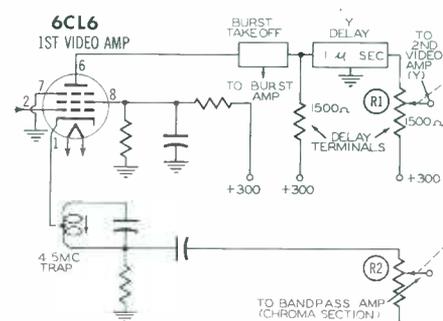


Fig. 14B. Location and Terminal Points of Y-Delay Line.

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- ★ Built-in 60 cycle sine-sweep phasing control.
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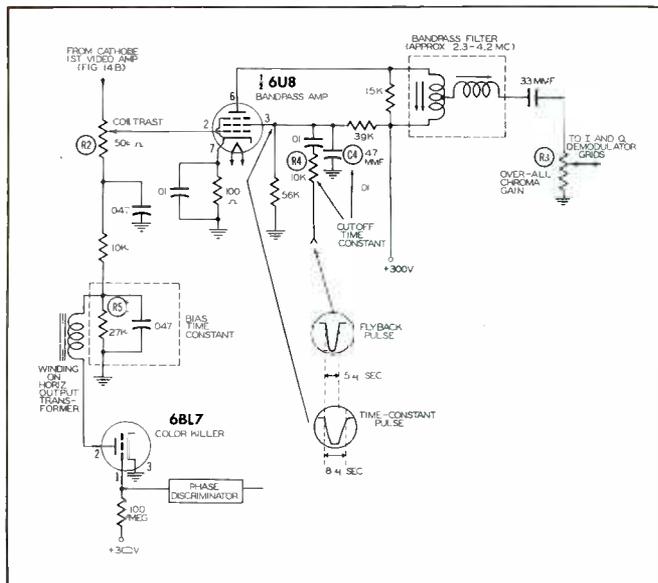


Fig. 14C. Bandpass Amplifier and Associated Circuits.

The amplified composite signal appears in the plate circuit of the bandpass amplifier where it is loaded by a filter which restricts the bandpass to approximately 2.3 to 4.2 mc. The color-carrier sidebands along with the higher Y-signal frequencies are passed, but the lower frequencies which include H and V sync pulses are eliminated.

The grid return of this amplifier is through R5 and C5. This network constitutes a bias time constant and is shunted by the color-killer triode

through a separate winding on the horizontal-output transformer. The grid of the 6BL7 is returned to a plus 300 volts and to a point on the color-sync phase discriminator. During monochrome transmission, no color burst is transmitted. The phase-discriminator circuit is inoperative, and no negative voltage is supplied to the grid of the color killer. The color killer will conduct because of the positive pulses which are applied to the plate of the tube. This conduction results in the charge of C5. The time constant of C5 and R5 is such that a negative voltage which is sufficient to cut off the bandpass amplifier will be maintained between conduction periods. By cutting off the bandpass amplifier, the possibility of spurious chroma response during monochrome transmission is eliminated.

For color signals in which the color sync burst is transmitted, the grid of the color killer is held negative by a potential developed in the phase discriminator from APC (automatic phase control) action. Since the tube then cannot conduct even with a positive plate, C5 is not charged, and the bandpass amplifier functions normally.

It is recalled from earlier discussion that it is advantageous to eliminate the color sync burst from the I and Q demodulation circuits and subsequent chroma amplifiers. This is shown, in the case of Fig. 14C, to be accomplished by feeding a negative pulse at H-flyback time to the screen of the 6U8. Since the flyback pulse is only approximately the duration of H-sync (5 microsec), it is necessary to delay or widen the keying pulse so that the negative screen holds past the occurrence of the color sync burst. In this circuit, R4 and C4 constitute a time constant sufficiently long so that

the charge of C4 through R4 holds the screen negative until slightly after the end of the color burst when active line scanning starts.

Burst Separator and Amplifier

It is necessary to separate the color sync burst from the composite video signal in order to drive the synchronizing section of the chrominance circuits. One method for doing this is illustrated by Fig. 14D.

The control grid of the burst amplifier receives the color burst through the tuned take-off transformer in series with the plate of the first video amplifier. Amplification of only the burst is assured by gating the cathode of the 6U8 at the proper time during the blanking interval. During the positive interval of the flyback pulse, the cathode remains too far positive to allow conduction of the tube. During flyback time, the pulse is negative and intercepts the conduction potential just before burst time. The cathode is held negative by the gate pulse (hence the tube is conducting) until just after the end of the burst interval. The gated color burst is amplified and fed to the phase discriminator through the tuned plate transformer.

* * Please turn to page 41 * *

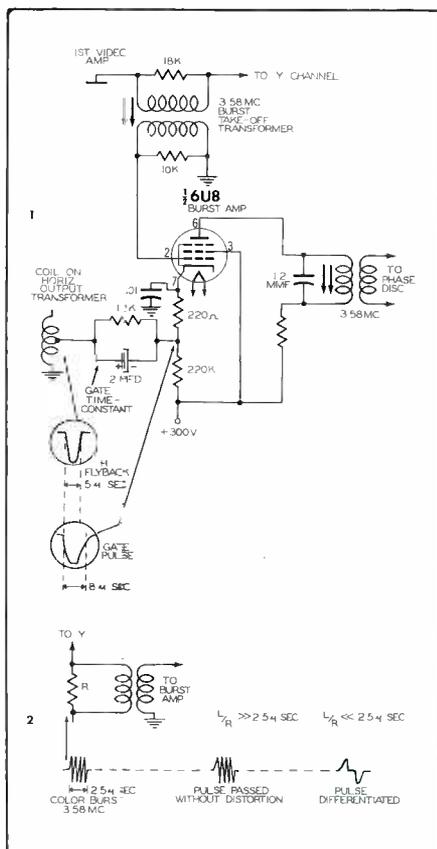


Fig. 14D. A Gated Burst Amplifier.

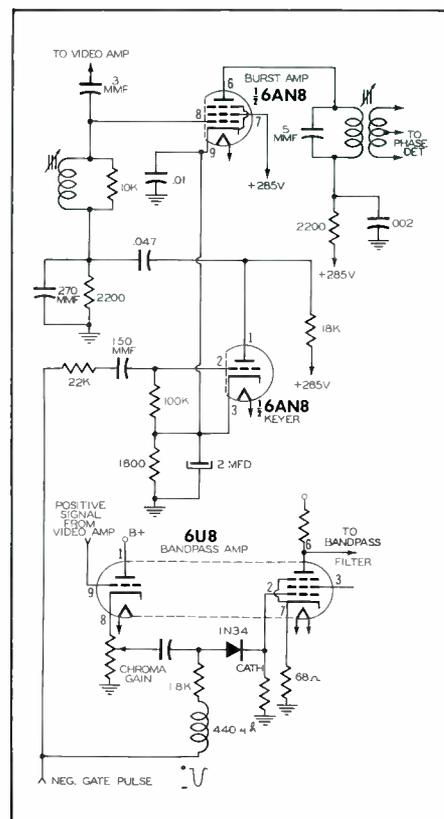


Fig. 14E. Gating Circuits for a Burst Amplifier and a Bandpass Amplifier.

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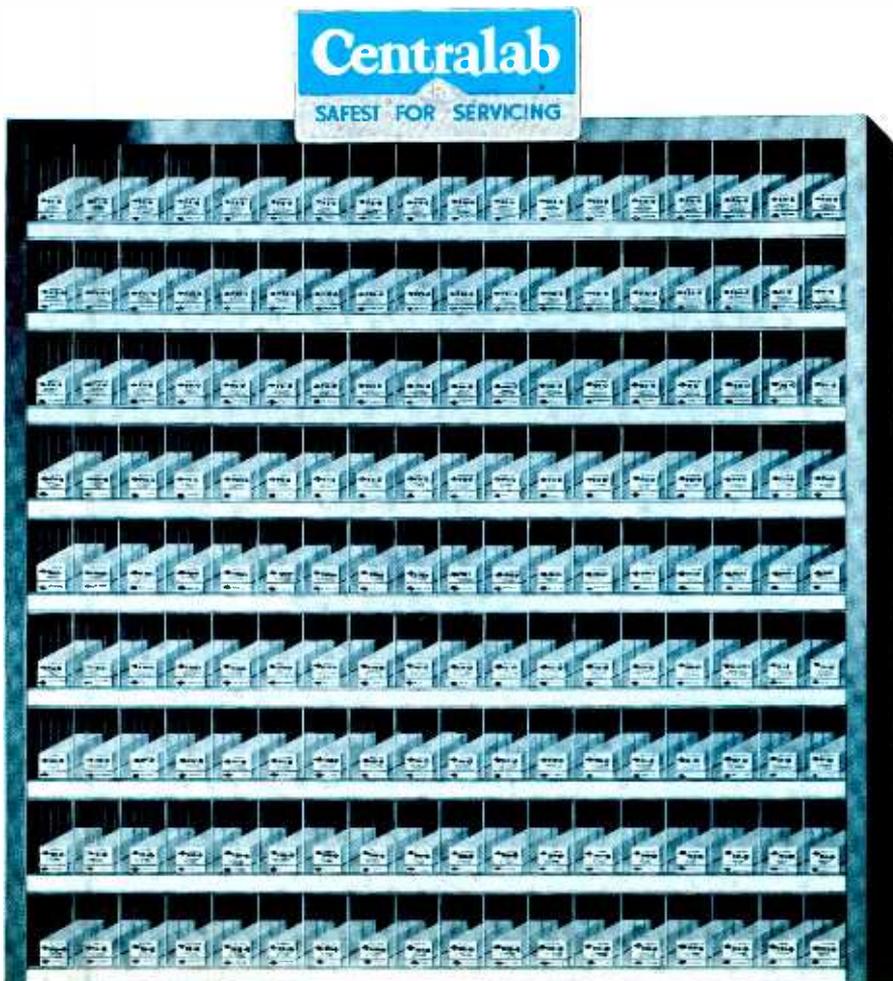
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AFC Circuits

Part IV The Gruen Circuit

by William E. Burke

This article which is the fourth of the series covers the operation of a phase detector, a capacitive reactance tube, a sine-wave oscillator, and a discharge tube when the combination of these stages is used to generate and control the horizontal sweep in a television receiver. The circuit which will be described is illustrated in the schematic of Fig. 8-25. Waveform numbers on the schematic identify points at which significant waveforms can be observed. The operation of the system may be explained through an analysis of these waveforms and the phase relationships between them.

The connection of the equipment for this analysis has been given in previous articles in this series, but it will be repeated here for the convenience of the reader who desires to follow the analysis by direct observation of the waveforms. In order to provide a suitable means of compari-

son between the various waveforms, the oscilloscope was synchronized externally with the saw-tooth voltage which is present at the grid of the horizontal-output tube. A 500,000-ohm resistor was included in series with this external sync connection so that the receiver operation would not be disrupted by loading of the circuit. By synchronizing the scope in this manner and by maintaining the frequency and amplitude of the horizontal sweep of the scope at constant values, we obtained all the waveforms with reference to approximately the same time base. Then, by the placement of associated waveforms one above the other, any change in either the frequency or the phase of these waveforms is made apparent. In addition, an isolation probe was used in the vertical-input lead to prevent the input capacity of the scope from affecting the receiver performance.

This system, like all other AFC systems, performs a comparison

between the received sync pulses and the horizontal-oscillator signal; and it controls the frequency and phase of the oscillator signal so that the signal will always be in the correct relationship with the sync pulses. The phase detector performs the comparison action and produces a DC voltage which is applied to the reactance tube. This tube then controls the frequency and phase of the oscillator. The oscillator output is applied to the discharge tube which generates the correct waveform for application to the horizontal-output tube.

Phase Detector

The phase-detector tube, V1 on the schematic of Fig. 8-25, requires two applied signals for its operation. These are a sync-pulse signal from the sync separator and amplifier and a feedback signal from the horizontal-output stage. The two signals are

* * Please turn to page 88 * *

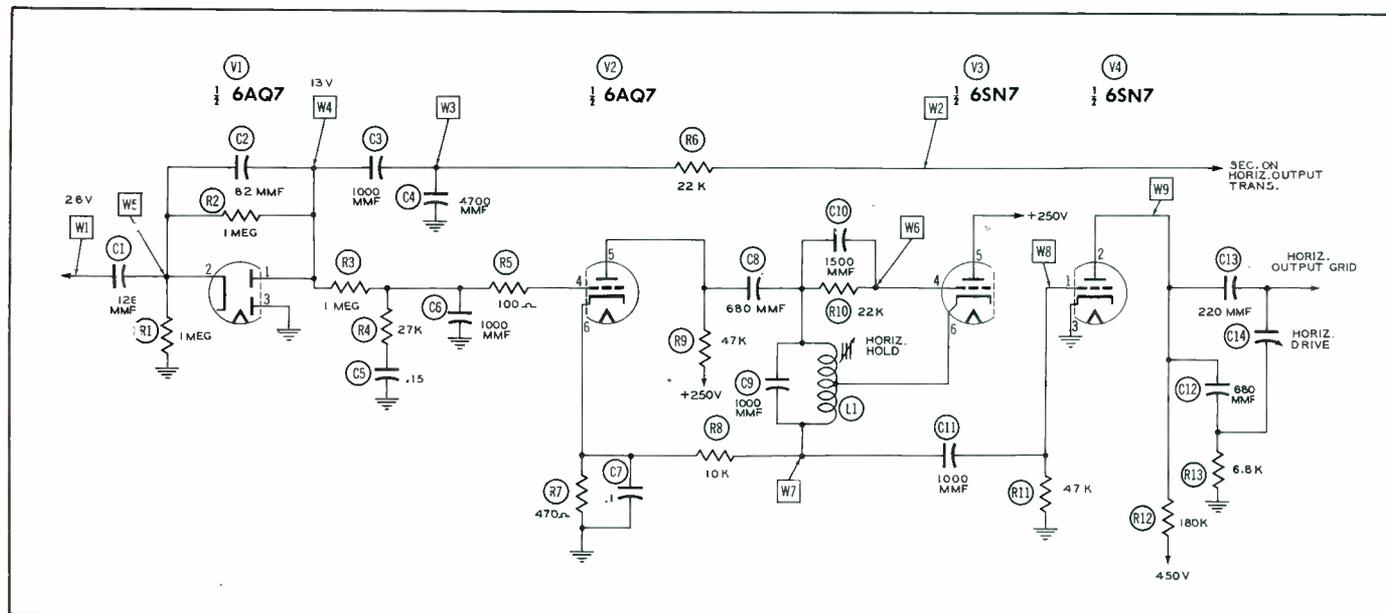


Fig. 8-25. Schematic of Gruen AFC Circuit.

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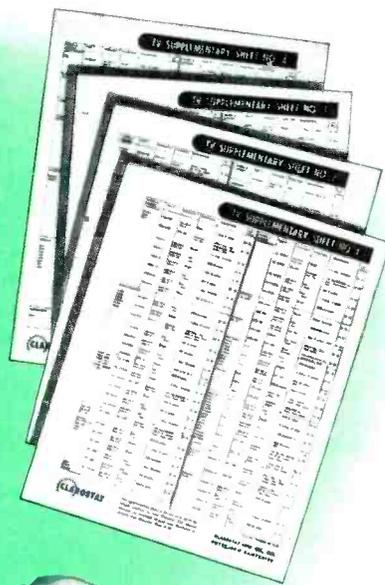
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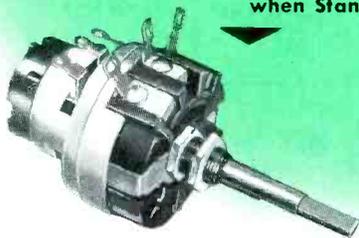


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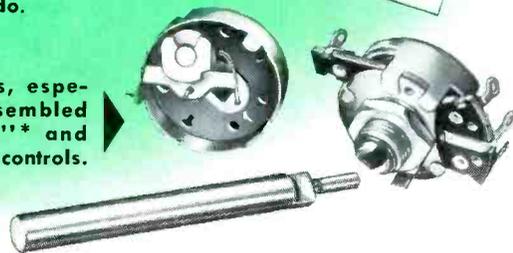
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A more detailed description of the equipment used in the Model RP-154 will show how carefully it has been designed to make it a complete system housed in one cabinet.

The large chassis (Fig. 2) combines the AM-FM radio tuner, the amplifier, and the power supply into one unit. The tuning dial, volume control, channel-selector switch, concentric tone controls, and tuning control are mounted on the front of the chassis.

The compensated volume control consists of dual potentiometers which aid in maintaining tonal balance at all levels of loudness. The ON-OFF switch is actuated by the volume-control shaft.

The independent bass and treble tone controls which are mounted concentrically provide a wide range of boost or droop for both the low and high frequencies. The amount of equalization made possible by the use of these controls is very useful because of the great variations in frequency balance encountered in records and other program material.

The four-position channel-selector switch permits easy selection of FM or AM radio reception, phonograph operation, or reception on an auxiliary channel marked SS (Special Service). This auxiliary channel provides for signal inputs from such sources as TV receivers and tape recorders.

The tuning control is used to tune the FM or AM receiver, depending upon the channel which is being used.

A ratio detector is used in the FM section of the conventional AM-FM receiver. Radiation from the FM oscillator is kept down to a very low level. Terminals are provided for an FM antenna, whereas a ferrite-rod type of antenna is featured in the AM section.

A 10-kc filter is included in the AM detector circuit to eliminate the 10-kc whistle (the beat between adjacent AM stations) which can be so annoying when one is listening with a high-fidelity AM receiver such as this.

Audio-Facts

The Capehart High-Fidelity Radio Phonograph Model RP-154

by ROBERT B. DUNHAM

Negative feedback is employed in the amplifier which uses two 6V6GT tubes in the output stage. The output is rated at 12.5 watts maximum power output. Distortion is held down to a very low percentage, and the extended frequency response is very smooth.

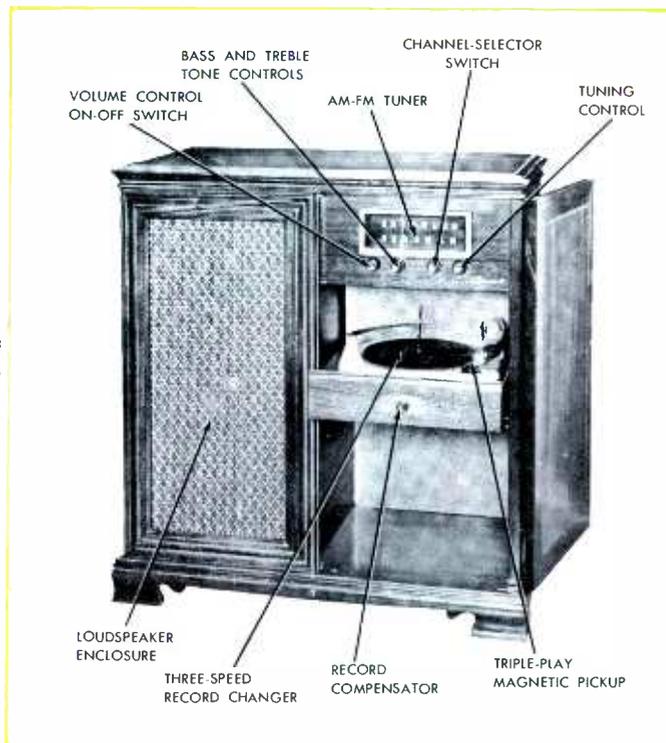
The three-speed record changer is a high quality unit featuring a weighted turntable, heavy four-pole motor, and a die-cast metal arm fitted with a plug-in magnetic cartridge. To avoid damage to the idler wheel while the changer is standing idle, the speed selector can be turned to its neutral position. This action disengages the idler wheel and removes the heavy pressure from its rim.

Incidentally, the control circuit in the amplifier is wired in such a manner that when the channel-selector switch is turned to the phono position, the supply of power to the complete system is controlled by the ON-OFF switch on the record changer. When the record changer automatically turns off at the finish of the last record (or is manually turned off) while the selector is set on phono, the complete system is turned off.

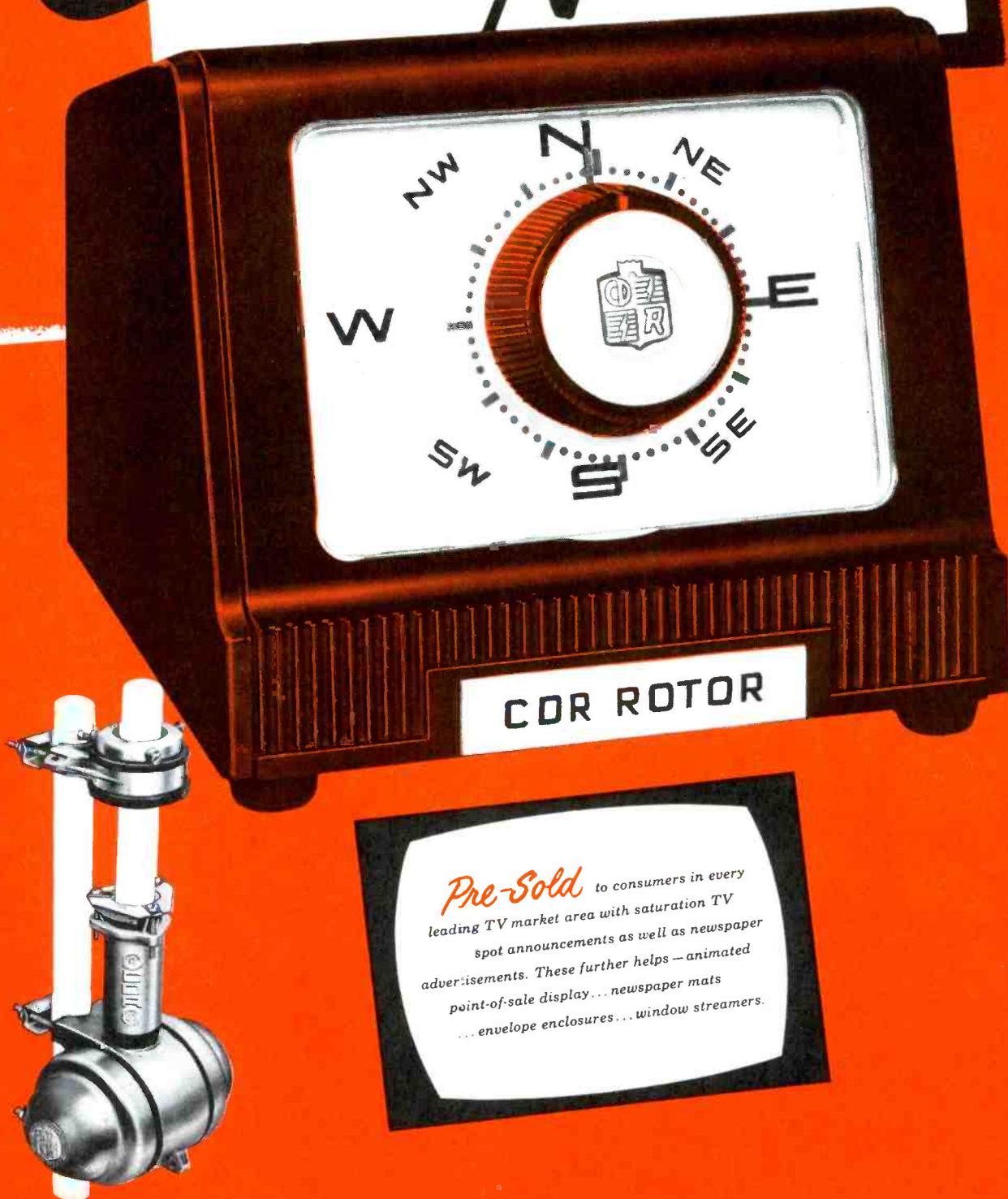
The phono preamplifier (Figs. 2 and 3) supplies the gain and equalization for correct operation of the magnetic pickup, which in this case

* * Please turn to page 86 * *

Fig. 1. Front View of Capehart Model RP-154.



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Models AR-1 and AR-2

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Model AR-1

... same as AR-2, without thrust bearing

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The heavy-duty rotor complete with handsome, modern design cabinet with meter control dial, uses 4 wire cable

Model TR-11

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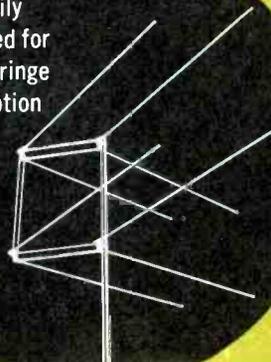
The new "Scotty" has every quality feature necessary for crystal-clear reception in metropolitan and suburban areas. Good gain and directivity on all VHF channels. Used effectively for UHF, or as a combination antenna. Tested and approved for color reception.

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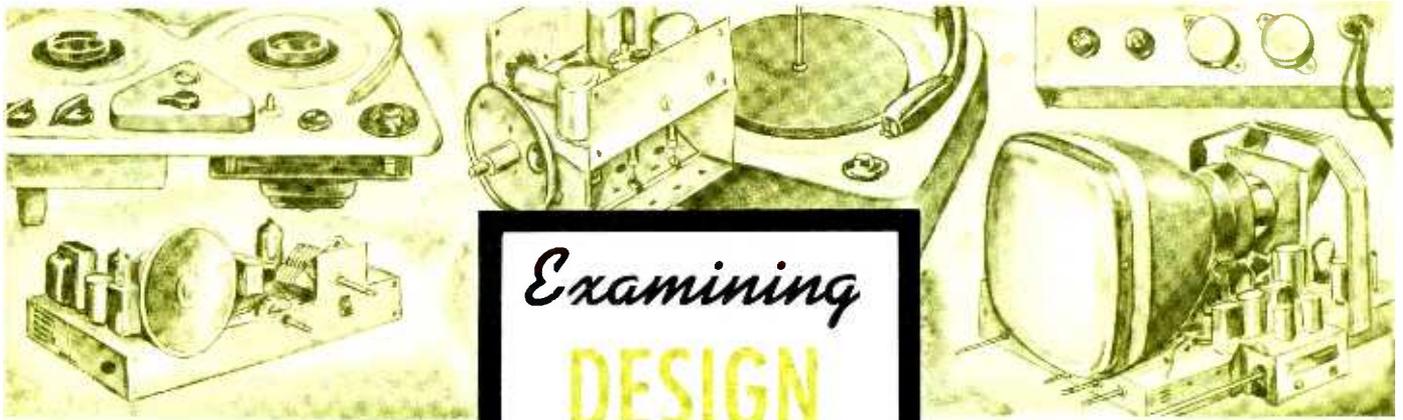


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GENERAL ELECTRIC MODEL 21C240

Recent trends in the General Electric line of receivers are exemplified by the Model 21C240. By investigating this model in detail, the service technician may become more familiar with current General Electric television receivers and consequently better prepared to service them.

The first feature that becomes readily apparent upon viewing the chassis is the familiar dip-solder method of assembly used in General Electric receivers. This may be seen in Fig. 1 which shows the chassis of Model 21C240. This receiver has a complement of nineteen tubes, exclusive of the 21AP4B picture tube. The video carrier IF is 45.75 megacycles, and the sound carrier IF is 41.25 megacycles.

The picture tube is mounted separately from the chassis by support brackets attached to the receiver cabinet. This permits the two units to be removed from the cabinet individually.

VHF Tuner

The RJX-062 is supplied for reception of the VHF channels 2 through 13. This is a switch type of tuner and has an input designed for 300-ohm lead-in. An IF trap is in-

cluded at the input of the tuner to eliminate interference from signals in the IF range. The adjustment for this trap is located on the top of the tuner. Proper adjustment is accomplished by tuning the trap for minimum interference. Care should be taken to see that the trap is not tuned into the range of channel 2.

The RF amplifier consists of a 6BQ7A dual triode connected in a cascode circuit. The grid bias of the first triode section is controlled by the AGC voltage.

The triode section of a 6X8 functions as the oscillator for the tuner. Individual frequency adjustments are provided for each channel. These adjustments are accessible without removing the chassis from the cabinet. The fine-tuning control is on a separate shaft connected to the tuner by a dial-cord arrangement.

The converter stage utilizes the pentode section of the 6X8. The output of the converter is fed to the first IF amplifier.



Fig. 1. The General Electric Model 21C-240.

Examining DESIGN Features

by DON R. HOWE

Video IF

Two traps are contained in the grid circuit of the first IF amplifier which is a 6CB6. One of the traps is tuned to 47.25 megacycles to provide attenuation of the sound signal in the adjacent channel. The sound signal in the tuned channel is attenuated by the other trap which is resonant at 41.25 megacycles.

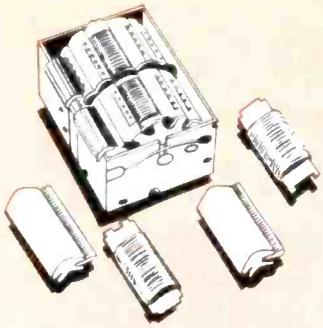
The second and third IF amplifiers are also 6CB6 tubes. Interstage coupling is accomplished by single-tuned transformers. In addition, these transformers are stagger tuned to achieve the desired bandwidth. The output signal from the third IF stage is transformer coupled to the video detector. The circuitry employed in the IF stages is conventional. The main difference between this IF strip and those used in some of the previous General Electric receivers is the tube complement. Some of these earlier receivers used lower-gain tubes with four IF stages in place of the present three stages which employ 6CB6 tubes.

Video

Video detection is accomplished by a Y151 crystal diode which is connected as a series detector. The output of the detector is fed to the 6CL6 video amplifier. Several video peaking coils are contained in the circuit linking the detector and the video amplifier. The cathode of the 6CL6 is returned to ground through a potentiometer which serves as the contrast control.

The plate circuit of this stage contains a 4.5-megacycle trap and two video peaking coils. The video signal is then fed to the cathode of the 21ZP4B picture tube. The cathode

* * Please turn to page 71 * *



G-C TUNER-KLEEN'R For every Standard Coil tuner. Cleans both stationary and rotary contacts at every twist of the channel selector. Easy to install, means extra profit, better reception.
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G-C SPRA-KLEEN The original power spray electrical contact cleaner and lubricant. Eliminates noises in TV tuners, contacts, controls, relays and switches. No waste, no need to remove parts.
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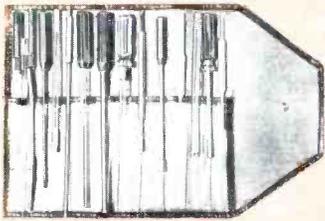
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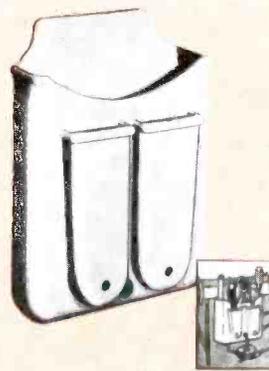
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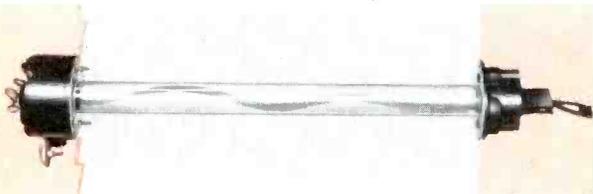
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Dollar and Sense Servicing

by

John Markus

Editor-in-Chief, McGraw-Hill Radio Servicing Library

WHALES. Down in Antarctic waters where whaling is a science, the catcher ship of a whaling fleet will shoot an explosive harpoon into a whale. Then they play the mamal with the three-inch nylon rope till it gives up and can be reeled in. If the catch is a blue whale that sinks after death, the next step is poking an air pipe into the whale and inflating it with thousands of cubic feet of compressed air. A tiny battery-operated radio transmitter is then shot into the whale's carcass, and the catcher goes off in search of another whale. The follow-up buoy boats are equipped with radio direction finders so they can go straight to the whale, even in darkness or fog. Then they tow it to the factory ship. For more of the story of how modern machinery operates today at the loneliest end of the earth, read the new book by R. B. Robertson, "Of Whales and Men."



ENIGMA. Round and round the wheel goes, and where it stops nobody knows. Such is roulette, and such is color television today. RCA announced it's stopping production of its 19-inch color tube, with intimations that something still better is in the offing.



SALES. The drop in radio sales for the first half of 1954 was baffling to manufacturers who'd learned to live right up to the 1952 and 1953 boom-year sales, but actually the change is far from world-shaking. Available figures for retail radio sales show 1,330,000 sets sold in the first four months of 1954, as compared to 1,850,000 for the same months of 1953 and 2,150,000 for those months in 1952.

Radio set inventories totaled about 3.5 million at the end of April this year, with 1.4 million of these on dealers shelves, 1.1 million in distributor storerooms, and about one million still stuck at the factories. This probably means you'll be seeing liquidation sales and price-cutting deals this fall, particularly among slower-moving models in the higher-priced brackets.



CHOPPER. One of the cutest new components we've seen lately is a photoelectric chopper which breaks up a weak and slowly varying DC signal into an AC signal that can be amplified more easily. All there is in the housing is a U-shaped neon flash tube and a tiny selenium photoelectric cell. The flash tube is connected to any 60-cycle power source of appropriate voltage, and the photocell is connected in series with the DC signal circuit. The repeated flashing changes the resistance of the cell 120 times a second to give the desired chopping action, and the AC signal is picked off across the cell. It's designed chiefly for use in guided missiles, in place of the vibrator type of choppers that don't always withstand the high-G shock of launching and the vibrations of flight. Avion Instrument Corporation in Paramus, N. J., is the manufacturer.

Incidentally, this firm has an ingenious array of desks for its engineers. They're made from flush panel doors, with one end resting on a two-section metal filing cabinet and the other end having feet made from 1 1/2-inch wood dowel rods fitting into drilled holes at a slight angle. Total cost is only a fraction of that of a new desk. Try one for your shop; oftentimes an odd-sized door can be picked up at a bargain. At a Chambers Street surplus store in New York City last year, you could take your pick from hundreds of them for \$10.95 each.

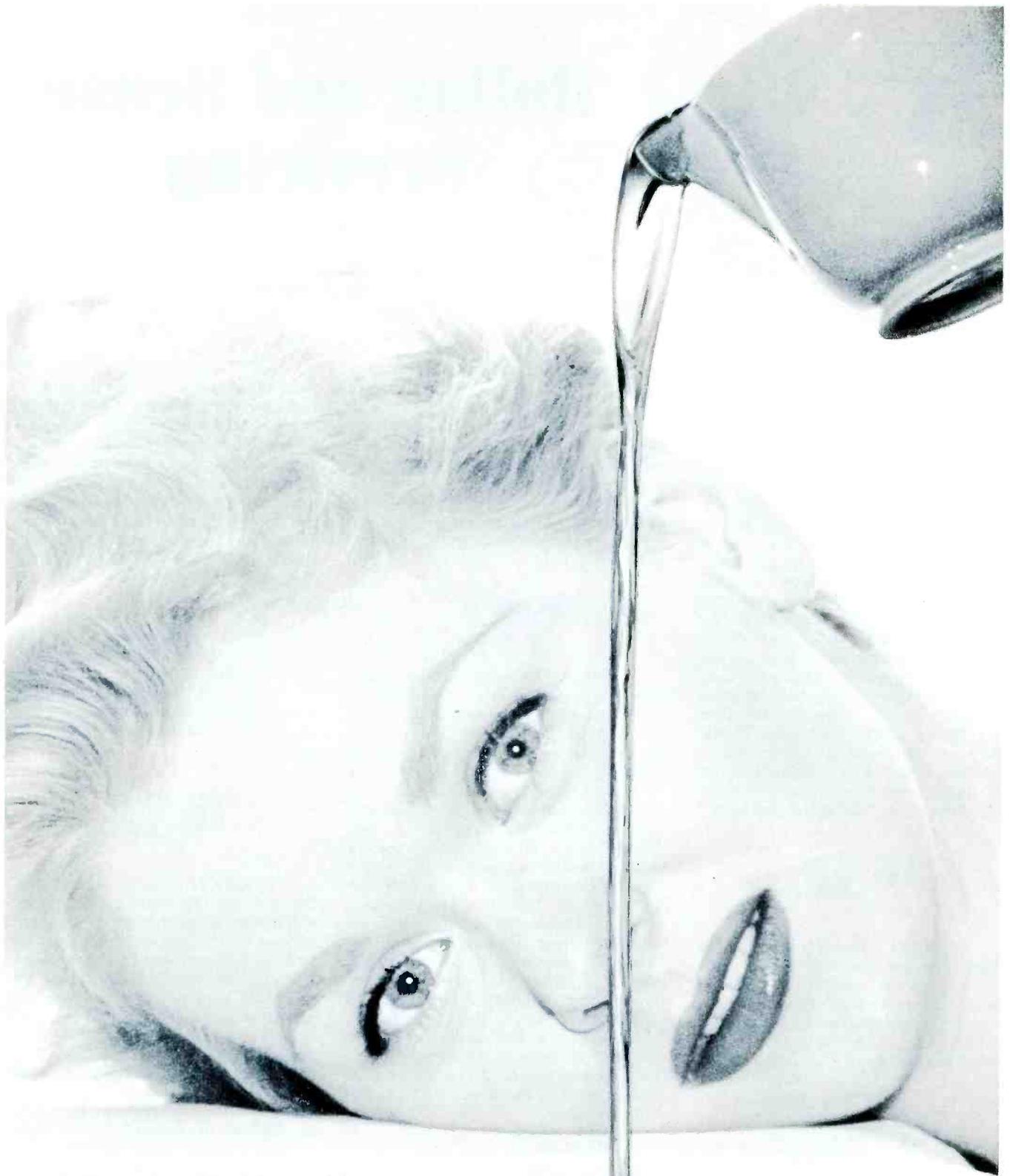
SCRAMBLER. For those who want to scramble up a telephone or radio conversation, the MX 595-6SQ-1A Speech Scrambler can be bought on the surplus market for \$45. It uses numbered code cards to insure complete privacy. It'll take another \$45 for a companion unit to unscramble the jibberish at the other end. These scramblers were advertised in June Electronics by V & H Radio & Electronics, 2033 W. Venice Blvd., Los Angeles 5, Calif.

Kinda reminds us of the IFF unit we spent twenty bucks for right after the war. It looked so pretty with its acorn tubes and other cute UHF components that we did not have the heart to break it up to salvage the parts.



PRIVATE EYES. Latest trick for getting the evidence needed for extracting a divorce from an errant spouse is industrial television. The private eye gets into the room somehow when no one is around and installs the TV camera of cigar-box size behind some concealing plant or behind a one-way mirror on a closet door, runs the wires to an adjoining room having the monitor receiver, then sets up a camera to snap shots off the screen. The detective can then relax in leisure in a comfortable chair, glancing occasionally at the screen to see how the action is coming, and reaching up at appropriate moments to snap the camera and rewind the film. Being in a separate room the click of the camera can't be heard by the performers. The TV camera is of course completely silent. Already two contested divorce actions have been settled out of court as a result of TV photos. Thus does television invade still another phase of our way of life.

* * Please turn to page 60 * *



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P.S. *This could be a sweet deal for you, too—
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TV Colormath

(Continued from page 27)

Fig. 14D, section 2, shows some waveforms which illustrate the effect that proper burst-transformer time constant L/R has on the pulse-passing characteristic. So long as L/R is much greater than the pulse duration, which is 2.5 microseconds, the color-burst envelope will be passed without distortion. Should L/R becomes less than this duration, with a radically increased R or decreased L , the envelope will be differentiated; and the color burst is lost.

Another method for extracting the color burst is shown in Fig. 14E. In this example, a negative gating pulse is fed to the grid of a keyer, is amplified, and is inverted in polarity. The resultant signal is fed to the grid of a burst-amplifier stage. The cathodes of the burst amplifier and the keyer are connected together. The heavy conduction of the keyer tube during scan time produces at the cathode a positive voltage which is sufficient to cut off the burst amplifier. The positive pulse which is fed to the grid of the burst amplifier is sufficient to overcome the bias voltage applied to the cathode, and the tube conducts. Thus, the color burst is extracted from the composite video signal and is passed to the phase-detector circuit.

Fig. 14E also illustrates a circuit which can be used to kill the color sync burst in the bandpass amplifier. The triode section of the 6U8 is employed as a cathode follower to feed the grid of the pentode section through a 1N34 diode. For the duration of the negative gating pulse, the positive terminal of this diode is held too far negative to allow conduction; and grid No. 1 of the pentode receives no signal. During intervals between gating pulses, the video which is of positive polarity at this point is passed and amplified. Since the gating pulse is usually taken from the horizontal-deflection system, it should be realized that the stability of the horizontal AFC is of great importance for color receivers. The phase of the gating pulse must not radically change over the normal range of the horizontal-hold control.

Color Sync and Phase

The output of the burst amplifier feeds a phase-detector circuit which also receives a signal from the local 3.58-mc oscillator. The phase detector has an output voltage which indicates by changes in polarity and magnitude any difference in phase of the two signals. This correction voltage is fed to a conventional reactance-

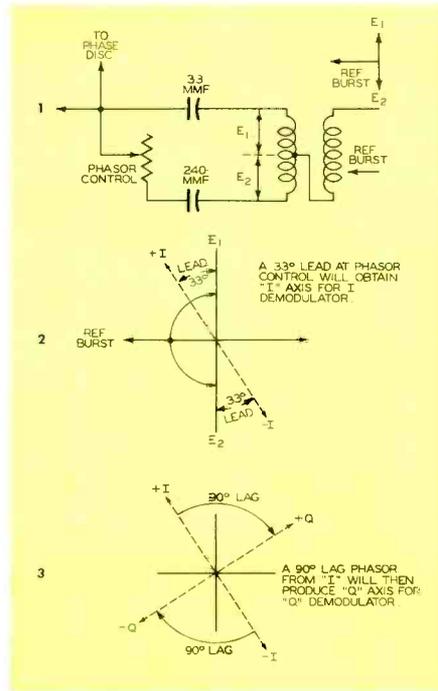


Fig. 14F. Phasing Requirements for the CW Signals to Enable Demodulation on the I and Q Axes.

tube circuit which locks the local oscillator on frequency and at a specific phase relationship with the transmitted color burst.

Before looking at typical circuits in this section of the color receiver,

let us review system requirements for the I and Q circuits. Fig. 14F aids in this review. Remember that a definite phase relationship is necessary so that I (wideband color) lies along the orange-cyan axis of the color triangle.

The voltage induced in the secondary of the transformer shown in section 1 of Fig. 14F will lag the primary reference-burst current by 90 degrees. This is conventional transformer action. Since this secondary is center tapped, voltages at opposite ends are 180 degrees apart. Thus, E_1 and E_2 are 180 degrees apart and in quadrature to the reference burst as shown in the phase diagram.

We may now see that (in Fig. 14F, section 2) if the voltages E_1 and E_2 are exactly in quadrature to the color-burst phase, adjustment of the phasor control (R-C combination which produces a leading phase angle) to 33 degrees will cause the output voltage to lie along the I axis. If E_1 and E_2 are not exactly in quadrature to the reference burst (as is usually the case due to leakage reactance), the phasor control covers an adequate range to provide proper phasing. This voltage is fed to the phase discriminator which compares it with the reference burst. A correction voltage will then hold the local oscil-

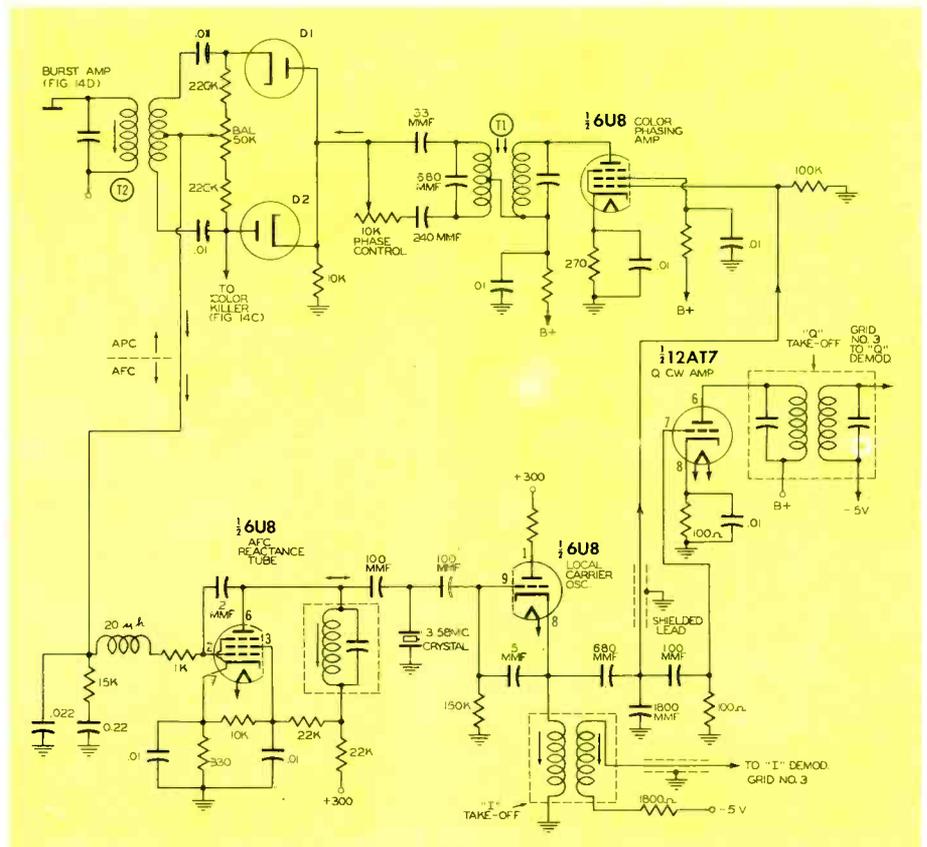


Fig. 14G. A Color-Synchronizing Circuit.

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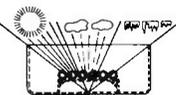
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lator at this phase angle (I axis), as described in the following.

Observe in Fig. 14F, section 3, that a 90-degree lag phasor from the I axis will supply a carrier along the Q axis. The importance of this lies not so much in practical adjustment of receiver circuits but in the fact that it enables a more accurate visualization of the system function. A phasing control, ordinarily on the front panel, properly phases the local oscillator so that the locally injected carriers fall on the I and Q chrominance-signal axes. Improper adjustment causes inaccurate color reproduction such as reds going blue, blues going green, and the like.

Fig. 14G shows one type of APC loop for color synchronizing. Diodes D1 and D2 constitute the phase-discriminator circuit for comparison of the local-oscillator signal through T1 with the transmitted burst signal through T2. Note that the diodes are connected to conduct on the same half-cycle of the signal. No conduction will occur without voltage from the burst amplifier.

Under conduction, the plate of D2 will go negative with respect to ground. This point connects to the color-killer grid (Fig. 14C) to prevent that tube from conducting during color telecasts.

Transformer T1 containing the phase control serves the function described in the foregoing. The discriminator will then act to supply a correction voltage for the reactance tube so that any deviation from the I axis is corrected as in conventional AFC circuits.

The inphase I carrier is taken off from the secondary of the transformer in the cathode circuit of the crystal oscillator. The Q amplifier feeds from the cathode of the oscillator.

Actually, APC circuits will vary widely. Some receivers use lumped resistance-inductance circuits for the quadrature phasing. Principles, however, remain the same.

The receiver which demodulates on the R - Y and B - Y axes differs from the one just described in that no 33-degree phase relationship with the reference burst is necessary. The B - Y signal lies along the sine axis. It is then only necessary to feed the R - Y demodulator through a 90-degree phasor to demodulate the red color-difference signal. This particular feature does not aid in simplification, since 33-degree networks are very simple (Fig. 14G); and

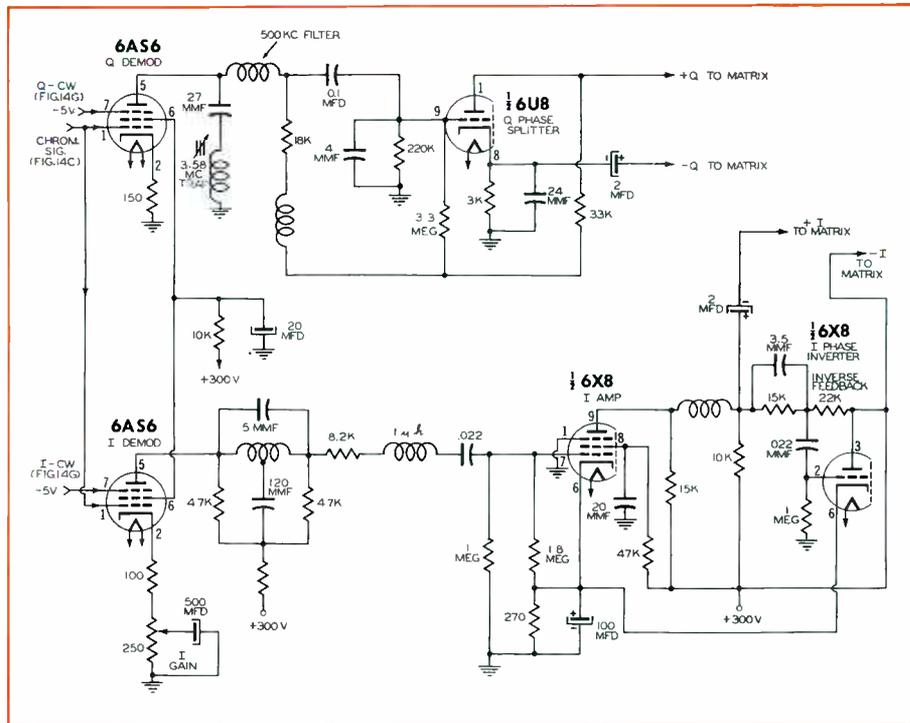


Fig. 14H. Demodulators and Phase Inverters for the I and Q Signals.

whether this 33-degree phasor is used or not, a phasing control must be used for accurate placement of the local-carrier phase.

Synchronous Demodulators

Fig. 14H illustrates one method of feeding the synchronous demodulators and the matrixer. The chrominance signal is fed to the control grids of the demodulators. The suppressor grid of the I demodulator is driven by the inphase CW, and the suppressor grid of the Q demodulator is driven by the quadrature CW. The chrominance signal, of course, contains both I and Q color information.

In the I demodulator, the output contains a vector sum of the I-signal sidebands from the chrominance channel and the inphase CW. The Q-signal sidebands in the chrominance signal, since they are in quadrature to the I sidebands, produce zero out-

put in the I demodulator. This is the action of a synchronous demodulator; the output is zero for components 90 degrees apart from the CW drive.

The output of the Q demodulator contains the vector sum of the quadrature CW and the Q-chrominance sidebands. The single sidebands of the I signal above 500 kc produce a quadrature component which will therefore crosstalk into the Q-demodulator output. This is the reason for the 500-kc filter in the plate load of the Q demodulator shown in Fig. 14H.

Note that the I demodulator has a gain control and an extra amplifying stage. Since the Q sidebands are equal (double sidebands), Q gain will be twice that of the I channel above 500 kc. The extra I amplifier compensates for this difference, and the gain control allows exact adjustment for proper gain ratio.

Fig. 14I illustrates the basic operation of a synchronous demodulator. Note from Fig. 14G that the suppressor grids (grid No. 3), which receive the CW signals, are biased at a negative 5 volts. The peak voltage of the CW signals may be approximately 30 volts. Parameters of the circuits are such that the tube conducts heavily on peak regions of the CW signal even though there is no chrominance modulation on grid No. 1.

The CW signal is shown in section 2 of Fig. 14I. Corresponding tube

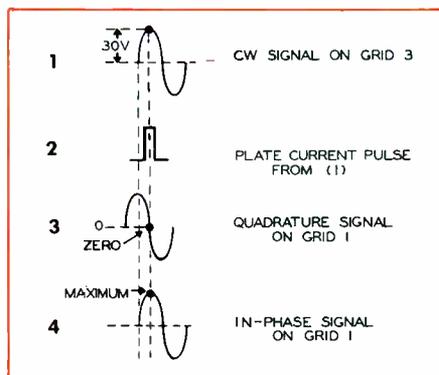


Fig. 14I. Synchronous Demodulator Action.

* * Please turn to page 47 * *

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—a high gain, wide band oscilloscope. Band width of 4.5 megacycles allows accurate display of video frequencies, including pulse wave forms and color synchronizing bursts. High sensitivity of 17 millivolts per inch makes it ideal for setting resonant traps, as a general null indicator, signal tracing in low level stages, phase measurements as well as for sweep frequency visual alignment of TV receivers. Has provisions for internal calibration, internal phased sine wave, and Z-axis intensity modulation. Reversal of polarity of both horizontal and vertical signals accomplished by means of toggle switching. Identical vertical and horizontal amplifiers . . . direct coupling used throughout.



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—for efficient trouble shooting and lab practice in problems of sound and video IF circuits, associated trap circuits, TV tuners, video amplifiers and all-purpose

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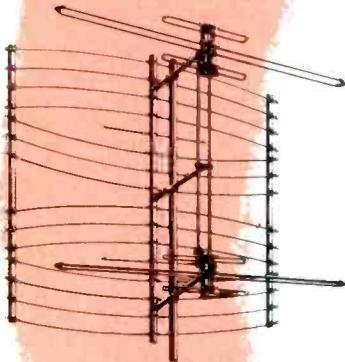
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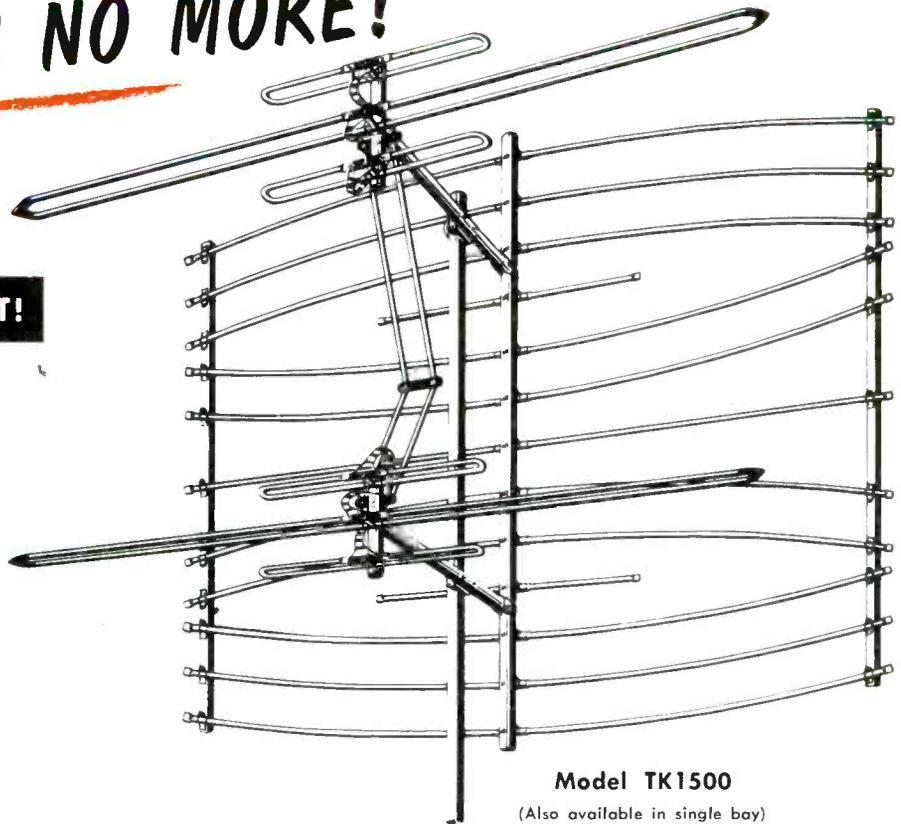
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TV Colormath

(Continued from page 43)

conduction with no chrominance signal is shown in section 2 of Fig. 14I. Any instantaneous signal voltage on grid No. 1 will determine the amount of that current that reaches the plate. Thus, the instantaneous voltage on grid No. 1 is multiplied by the instantaneous voltage on grid No. 3. This action is sometimes referred to as product demodulation.

On grid No. 1, signals that are inphase will go positive when grid No. 3 goes positive. This results in heavy plate current on the positive peaks. The pulses will follow modulation on grid No. 1.

A quadrature signal on grid No. 1 (section 3 of Fig. 14I) will be zero at the time of plate current pulse, therefore no signal is produced in the output. An inphase signal (section 4 of Fig. 14I) will add vectorially to the CW signal.

If the CW signal is not the same frequency and phase as the chrominance signal, the usual superheterodyned beat frequency results. This undesired beat component will be modulated by the amplitude variations on grid No. 1, and as a result there will be spurious products in the output circuit. The fact that these signals pass through the low-pass filters into the chrominance amplifiers emphasizes the importance of proper APC loop-phasing adjustments.

Note that the plate of the Q phase splitter (Fig. 14H) is DC coupled

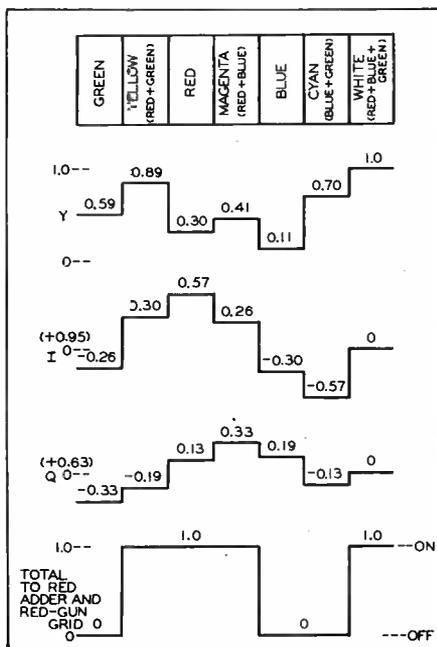


Fig. 14K. Voltages at Red Matrix for Indicated Bar Pattern.

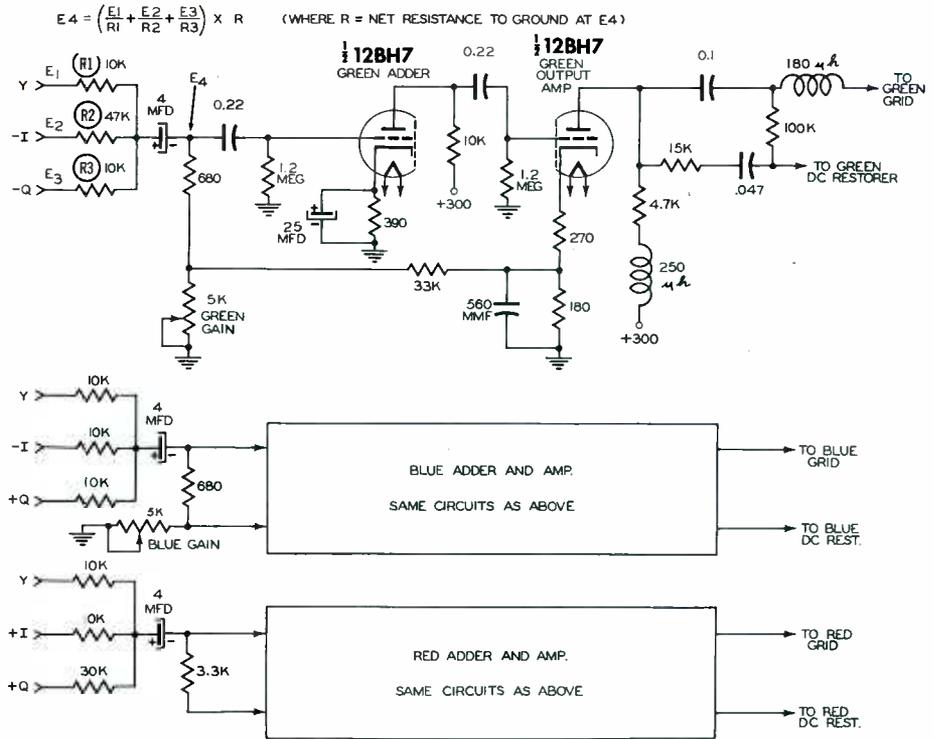


Fig. 14J. Color Matrix, Adder, and Output Circuits.

to the matrixer while the cathode is AC coupled. This is necessary to isolate plate and cathode DC voltages in the matrix. Similarly, the +I signal DC coupled and the -I signal DC coupled to isolate these separate voltages. The I phase inverter contains negative feedback which holds the output amplitude equal to the +I amplitude. Thus, the tube acts only as a polarity inverter.

Matrix and Adder Circuits

Fig. 14J illustrates typical matrixer and color-adder circuits. Identical circuits are employed in

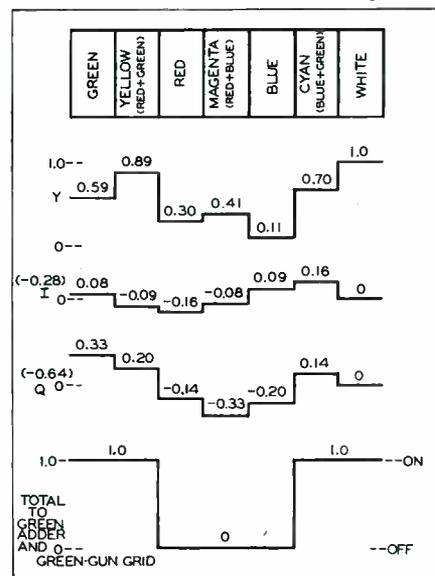


Fig. 14L. Voltages at Green Matrix for Indicated Bar Pattern.

this example for the red, green, and blue adders and amplifiers. The three output circuits are employed to obtain unequal signal drives which are necessary to compensate for phosphor efficiencies. Red phosphors require maximum signal drive, green less, and blue the least. The green and blue gains can be adjusted so that the proper signal drive is obtained.

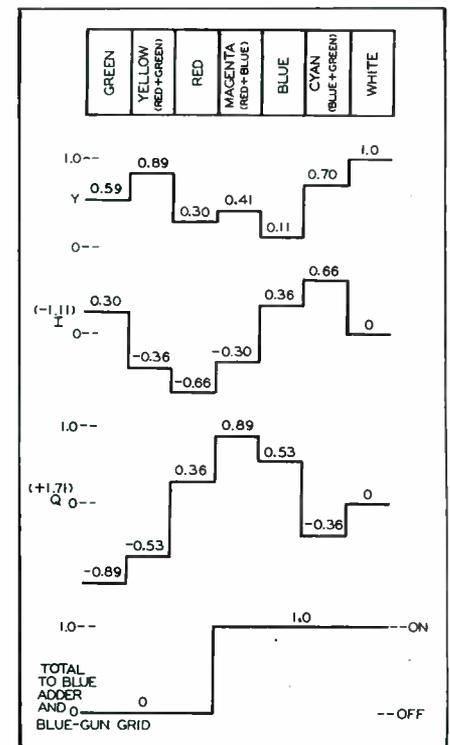


Fig. 14M. Voltages at Blue Matrix for Indicated Bar Pattern.

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TABLE II
EFFECTS OF LOSS OF THE I SIGNAL

	Values Existing in the Color Channels											
	Green Bar		Yellow Bar		Red Bar		Magenta Bar		Blue Bar		Cyan Bar	
	Normal	Without I	Normal	Without I	Normal	Without I	Normal	Without I	Normal	Without I	Normal	Without I
Red Channel	0	0.26	1	0.70	1	0.43	1	0.74	0	0.30	0	0.57
Green Channel	1	0.92	1	1.09	0	0.16	0	0.08	0	-0.09	1	0.84
Blue Channel	0	-0.30	0	0.36	0	0.66	1	1.30	1	0.64	1	0.34
Effects Caused by the Foregoing Conditions												
Red Channel		0.26		0.70		0.43		0.74		0.30		0.57
Green Channel		0.92		1.09		0.16		0.08		0		0.84
Blue Channel		0		0.36		0.66		1.30		0.64		0.34
Colors Reproduced		Contaminated yellow-green		Yellow-green		Desaturated magenta		Purple		Purple at low brightness level		Yellow-green

Note, however, that the red channel has no gain control. Adjustment of the red channel is not required, since the proper ratio can be obtained through adjustment of the green and blue gains.

To enable a clear visualization of matrixer action, the graphs of Figs. 14K, 14L, 14M, and 14N are presented.

Observe Fig. 14K, which is a graph showing voltages at the red matrix (and red-gun grid) for the indicated bar pattern. For example, we know that the red phosphor will be biased off for a green signal. Note that on the green bar (indicated at top of graph), Y is 0.59; I is -0.26; and Q is -0.33. The total is zero, as indicated on the bottom curve. Also note that for the red bar and for bars which combine red with another color, the totals add to give unity. The values for the green and blue mat-

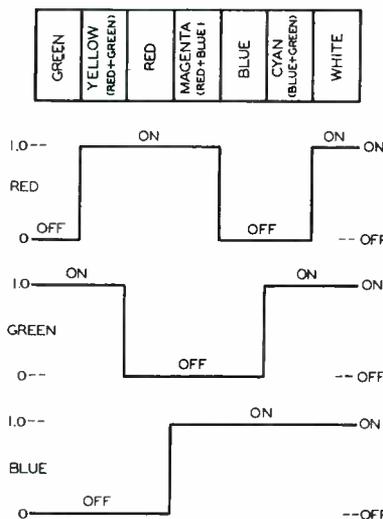


Fig. 14N. Combined Action of the Three Primary Channels for Reproduction of Indicated Bar Pattern.

rixers are shown similarly by Figs. 14L and 14M.

The combined action is shown by Fig. 14N.

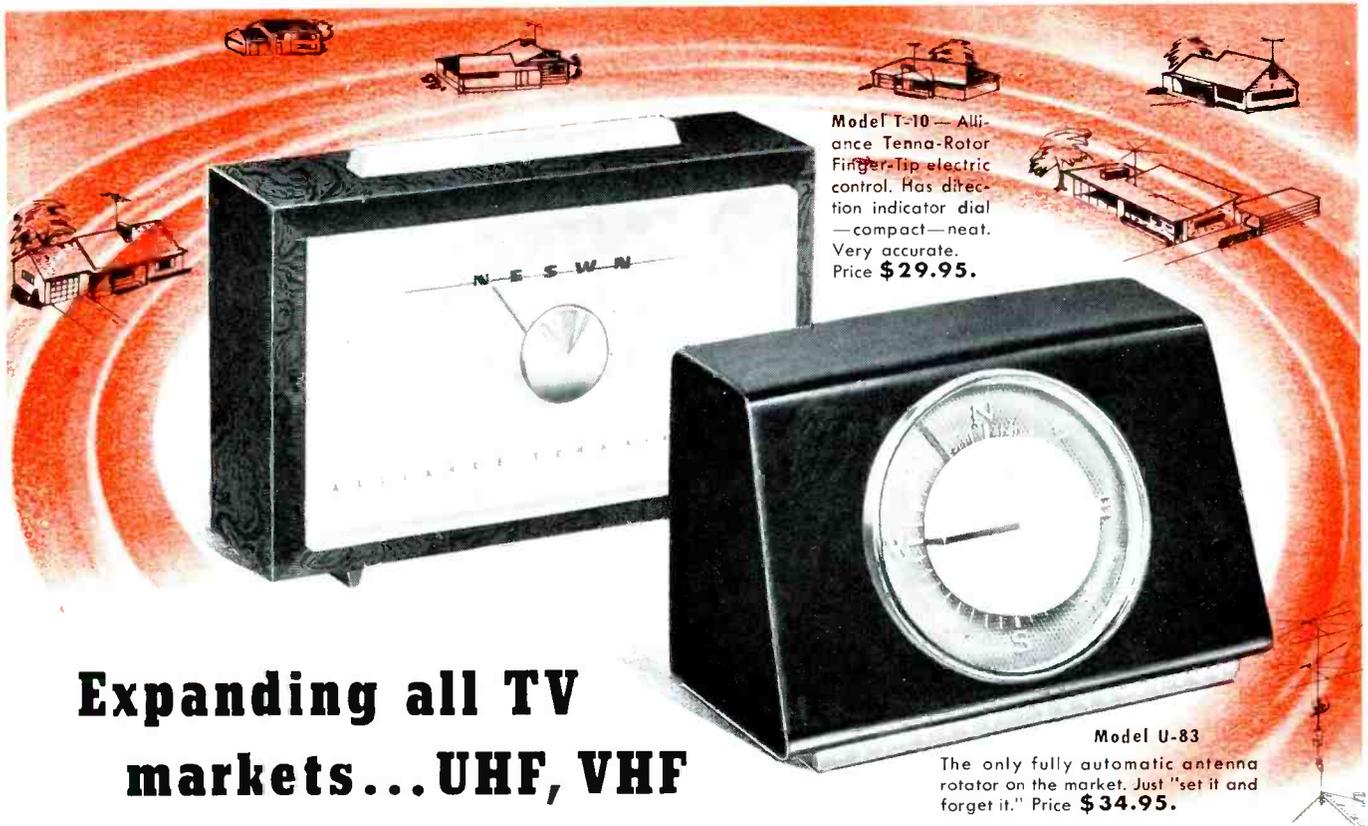
From observation of these graphs, we have prepared Tables II and III to note the results of loss of I or Q signals. Other tables could be constructed to show the effect of loss of any single color channel, change in values of matrix resistors, or the like.

As an example of use of the tables, note Table II for loss of I signal. The reader should check back through the graphs to see how these values are derived. Note that green without the I signal gives a final value of 0.26R, 0.92G, with blue biased off. The normal value is 1G, with red and blue biased off. Since some red is mixed with green in this example, the green bar will be reproduced as a contaminated yellow-green.

It is important that all amplifiers be as nearly linear as possible.

TABLE III
EFFECTS OF LOSS OF THE Q SIGNAL

	Values Existing in the Color Channels											
	Green Bar		Yellow Bar		Red Bar		Magenta Bar		Blue Bar		Cyan Bar	
	Normal	Without I	Normal	Without I	Normal	Without I	Normal	Without I	Normal	Without I	Normal	Without I
Red Channel	0	0.33	1	1.19	1	0.87	1	0.67	0	-0.19	0	0.13
Green Channel	1	0.67	1	0.80	0	0.14	0	0.33	0	0.20	1	0.86
Blue Channel	0	0.89	0	0.53	0	-0.33	1	0.11	1	0.47	1	1.36
Effects Caused by the Foregoing Conditions												
Red Channel		0.33		1.19		0.87		0.67		0		0.13
Green Channel		0.67		0.80		0.14		0.33		0.20		0.86
Blue Channel		0.89		0.53		0		0.11		0.47		1.36
Colors Reproduced		Purplish blue		Reddish yellow		Orange		Orange-red		Cyan		Blue-purple



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Model Genie-1

ALLIANCE MANUFACTURING COMPANY, Alliance, Ohio

Headsets for TV

(Continued from page 11)

has no effect upon the sound being produced by the speaker. Second, the circuit uses a separate volume control, the setting of which has no effect on the speaker circuit. Third, it contains a tone control which also does not affect the speaker circuit. Fourth, the circuit will provide enough drive to operate several pairs of headsets. This makes it ideal for use in a hospital room where, more than one person may want to watch a show without disturbing others and for home use where more than one child will want to enjoy the afternoon cartoon without disturbing mother's afternoon bridge party. Safety for users of the headsets is assured because the headsets are isolated from the subchassis and from ground by the output transformer T1.

A 6AB4 high- μ triode is used as the audio amplifier. The input to this tube is obtained through a socket connector from the high side of the volume control in the receiver. Filament and B+ voltages are also provided through the socket connector. The input impedance of the 6AB4 is sufficiently high that it places a negligible load on the volume-control circuit in the receiver. A tone-control circuit consisting of capacitor C2 and potentiometer R3 shunts the plate load of the tube. The transformer T1 should have a primary impedance of 10,000 ohms and a secondary impedance equal to 500 ohms. The latter specification is based on the assumption that four jacks are incorporated and that the impedance of each headset is approximately 2,000 ohms. The jacks are the closed-circuit type.

The circuit in Fig. 1 may be modified to provide a constant output impedance by using a 2,000-ohm T-pad in place of the volume control on the headset. If closed-circuit jacks are not available, open-circuit jacks may be used. In this case, a 500-ohm resistor is connected across the

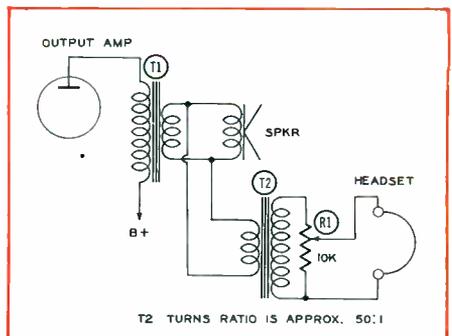


Fig. 2. Connecting a Headset to a Speaker by Means of a Second Transformer.

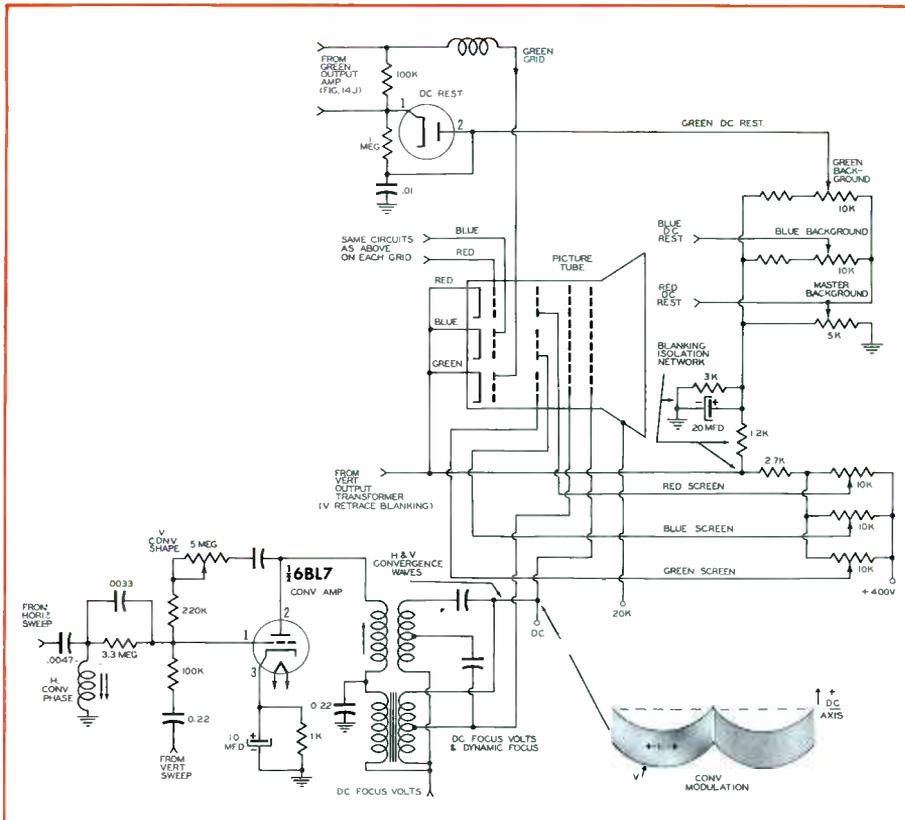


Fig. 14-O. Dynamic-Convergence Circuits, Screen and Background Controls.

Remember that the actual signals received are gamma-controlled to compensate for phosphor power-law characteristics. Should the amplifiers depart from linear amplification, the gamma-corrected signals will be distorted either to nullify or to over-emphasize the correction.

Color Picture Tube Circuits

Fig. 14-O designates the circuits associated with a three-gun color picture tube.

Each grid receives excitation from its specific video channel (Fig. 14J), is DC controlled, and is returned through individual background controls.

The cathodes are driven positive during vertical-blanking intervals by pulses from the vertical-output transformer. This assures complete retrace blanking.

Each screen can be adjusted in DC voltage by individual controls to aid in balancing phosphor efficiencies.

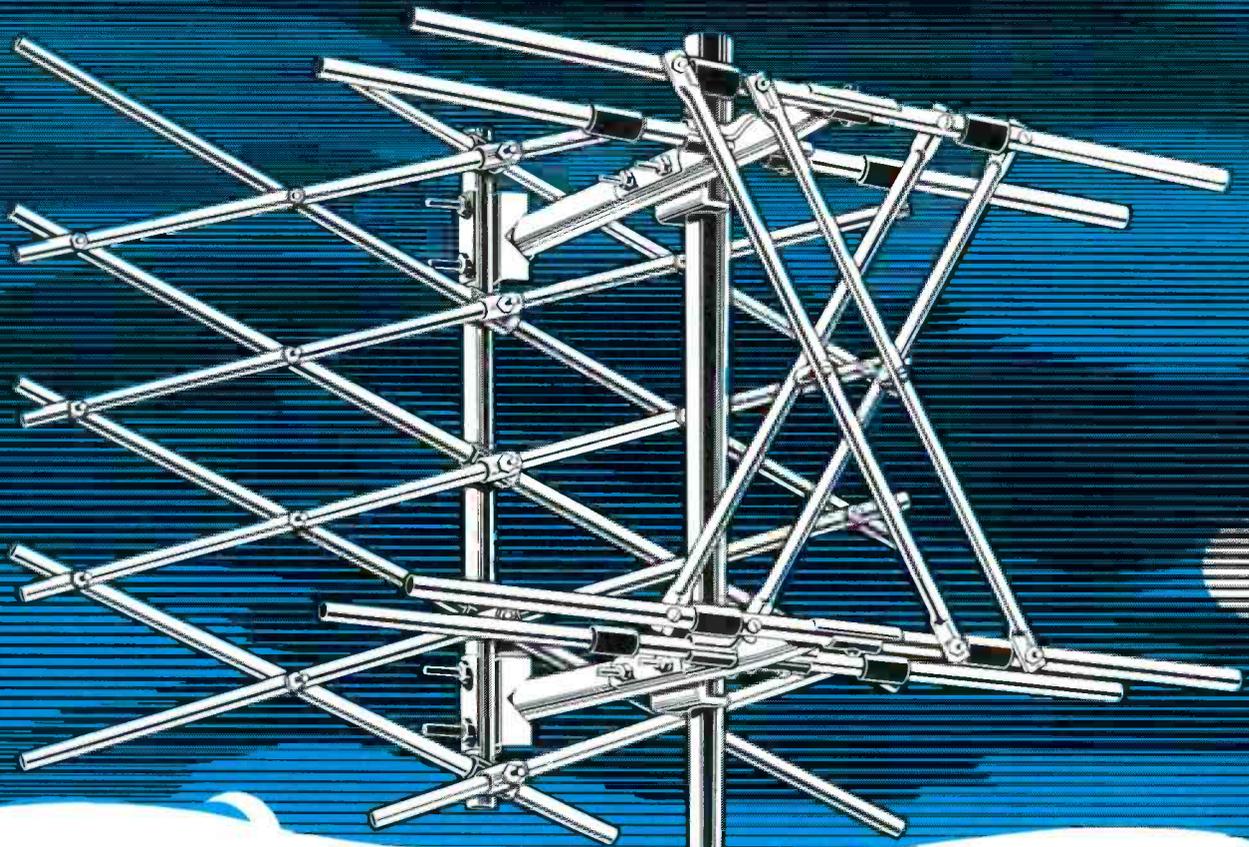
The convergence-amplifier grid receives horizontal and vertical waveforms from the cathodes of horizontal and vertical-deflection amplifiers. Shapes of the waveforms at these points closely approach a parabola. The controls that are shown shape the applied voltages properly to any correction necessary. The amplified

output modulates the DC applied to the convergence electrode. Since the distances from the guns to the top, bottom, left, and right regions of the screen are greater than the distance to the center of the raster; the beams from the three guns would not properly register without correction. Dynamic convergence corrects the applied voltage in step with the scanning position of the beams.

DC applied to the focusing electrode is adjustable for optimum control of the scanning-spot size from each gun. The focusing electrode also receives a portion of the parabolic waves to maintain focus during scanning.

The picture-tube high voltage is regulated by a shunt-regulator tube across a flyback voltage-doubler power supply. During a black picture and blanking intervals when no beam current is drawn, the regulator becomes the power-supply load. For a maximum white picture, the kinescope becomes the load and the regulator tube absorbs very little power. This method maintains constant load on the high-voltage power supply and allows good regulation for the picture-tube anode.

Harold E. Ennis



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secondary of T1 to replace resistors R4, R5, R6, and R7.

Fig. 2 illustrates a circuit hookup which has proved very satisfactory as a simplified circuit; however, there is still the expense of an output transformer. This circuit, too, contains a volume control which has very little effect upon the volume of the speaker output because of the relatively high impedance in the secondary circuit of transformer T2. This hookup is a fairly good one for a family which has one member who has difficulty in hearing over most of the audio range.

The circuit of Fig. 2 merely consists of a second transformer connected in such a manner as to step up the amplitude of the audio so that enough audio is available to be controlled. The transformer used for this purpose should have one winding of approximately 50 ohms in impedance. The second winding should have an impedance of approximately 10,000 ohms. There are certain inexpensive transformers having their principal applications in transceivers and inter-communication devices that will function satisfactorily as transformer T2. Since the headset circuit in Fig. 2 is isolated from the receiver by transformer T2, shock hazards to the user are eliminated.

A method of installing headsets in a case where they are to be used solely for the purpose of hearing in privacy is shown in Fig. 3. This circuit contains a closed-circuit phone jack in the plate circuit of the audio-output tube. When the headset is plugged in, the lead to the speaker transformer is broken and the headset transformer becomes the sole plate load on the output tube. If a family has more than one person who will be using headsets at the same time, these headsets could be connected in much the same manner as the secondary portion of the circuit in Fig. 1.

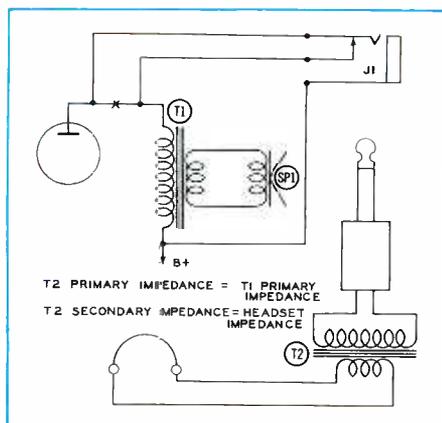


Fig. 3. A Method of Substituting a Headset for the Speaker.

The primary impedance of the headset transformer should be the same as that of the speaker transformer. The secondary will depend upon the number and impedances of the headsets. For instance, if four pairs of headphones are to be used and each pair has an impedance of 2,000 ohms, the secondary of the transformers should be 500 ohms.

Fig. 4 illustrates one of the less expensive hookups for operating a headset. The chief advantage to this circuit is its low cost. The disadvantages are more numerous. For example, changing the volume of the headset causes a change in the tone of the speaker, and the tone in the headset also changes with different volume settings. Furthermore, this circuit cannot be safely used with sets which have one side of the AC line connected to the chassis ground; there is a shock hazard because one side of the headset is also grounded. Finally, only one headset can be used with this circuit since the addition of

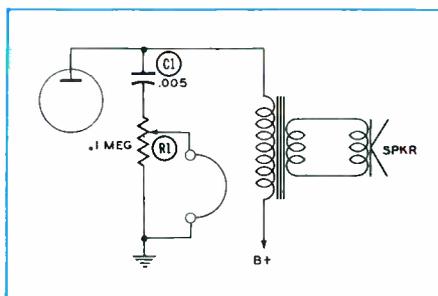


Fig. 4. A Transformerless Headset Connection.

others in parallel would require a higher setting of volume control R1 with a consequent reduction in the plate load on the output tube and a very pronounced effect on the volume and tone of the audio output. By the same reasoning, it would not be advisable to use a pair of very low-impedance earphones in a circuit of this type, because the tone of the speaker would be too greatly affected.

Of all the different ways in which a pair of headphones may be connected to a set, probably the least desirable is that shown in Fig. 5. This is especially true if the headphones have a fairly large impedance. For instance, if the equipment were to be used by a person who is partially deaf, a headset with an impedance of 2,000 ohms would produce such low volume that in order to hear satisfactorily, the wearer would have to turn up the receiver volume to such a point that it would be annoying to others who might be trying to listen to the speaker. Such a hookup is also a shock hazard if the secondary of

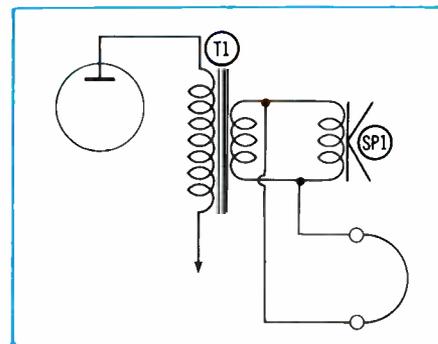


Fig. 5. The Simplest Method of Connecting a Headset.

the audio-output transformer is grounded and one side of the line is connected to the chassis ground.

What Type Headsets?

There are many types of headsets from which the set owner can choose. The choice will depend upon a number of things: the cost, how the set is to be used, the quality desired, and the wearing comfort and freedom of movement desired by the customer. Because there are so many from which to choose, it would be a good idea for the service technician either to carry several types in stock or to have some literature that the set owner might study to make his selection.

There are several types of light-weight headsets available; two of these are the Monoset and the Twinset manufactured by Telex, Inc. The Monoset is an inexpensive under-the-chin type with very small and light earphones which place very little pressure on the ears. The Twinset is also a very light unit and has the added feature of not placing any pressure on the ears. Instead, the receivers rest lightly on the temples, and two small tubular arms pipe the sound directly into the ears.

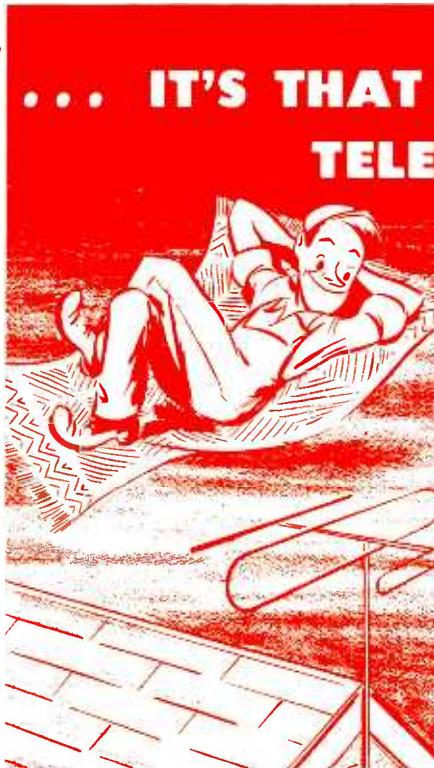
High-fidelity headsets are available and provide a very good quality of reproduction. However, they are quite expensive and are impractical for TV use by the average set owner.

Length of Lead

From an electrical standpoint, the length of lead is not critical. It should be made long enough that it will reach the point normally used for viewing without being stretched. It should not be so long, however, that it becomes cumbersome and a nuisance to put away when not in use.

HENRY A. CARTER

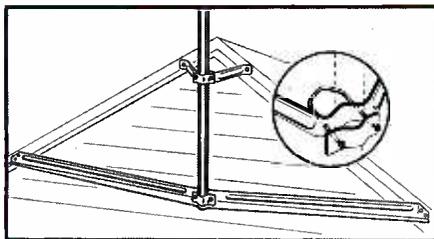
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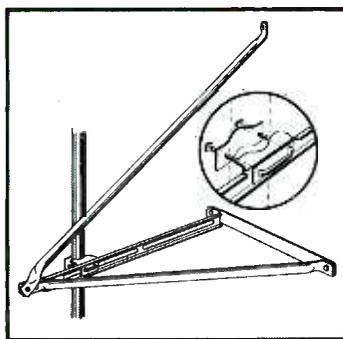
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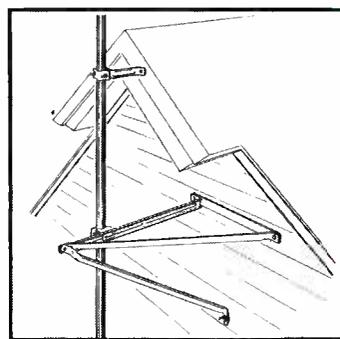
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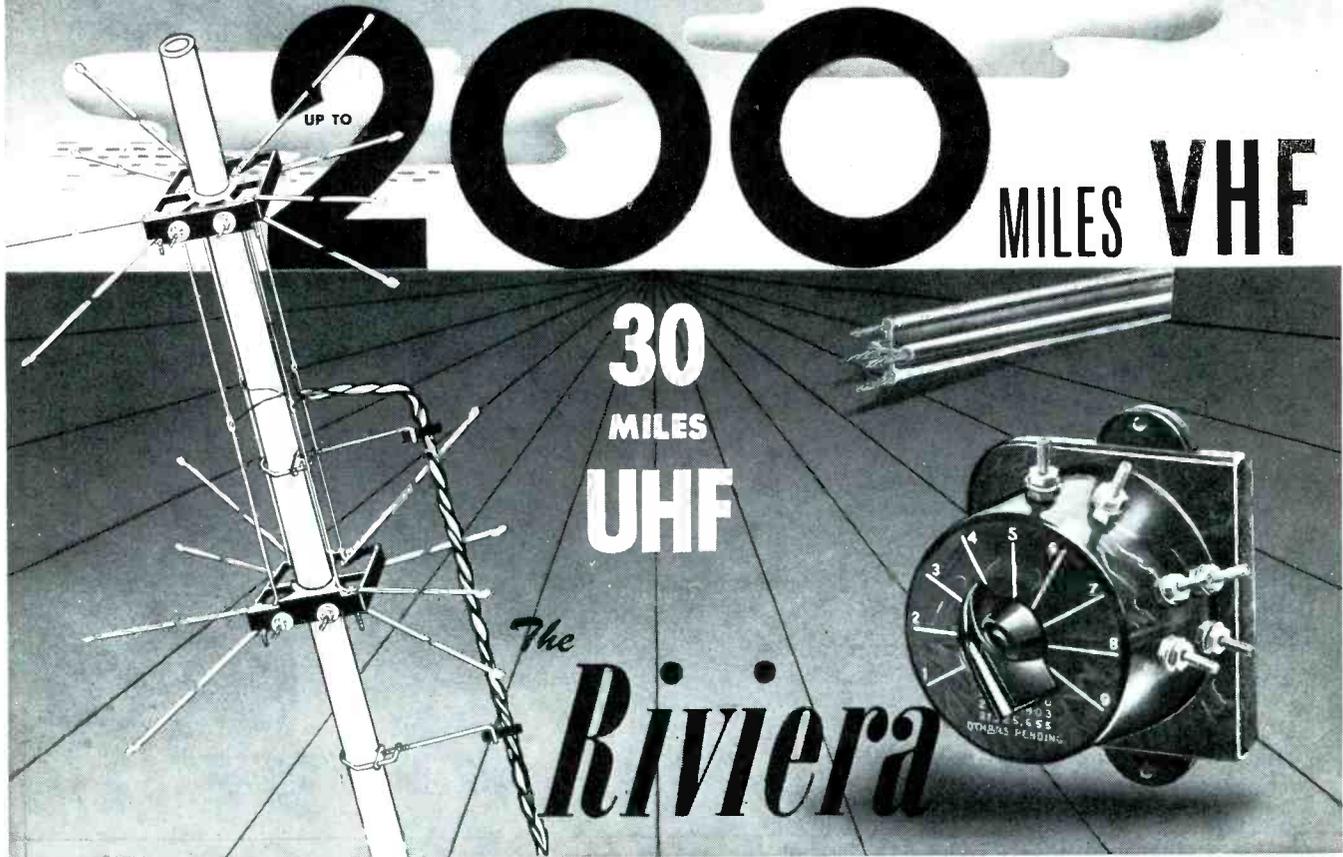
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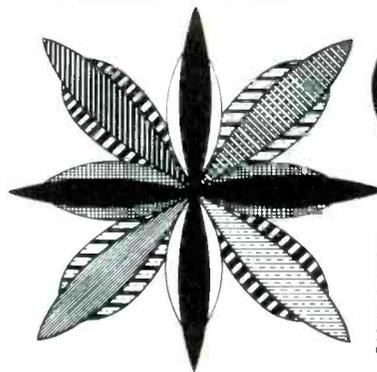
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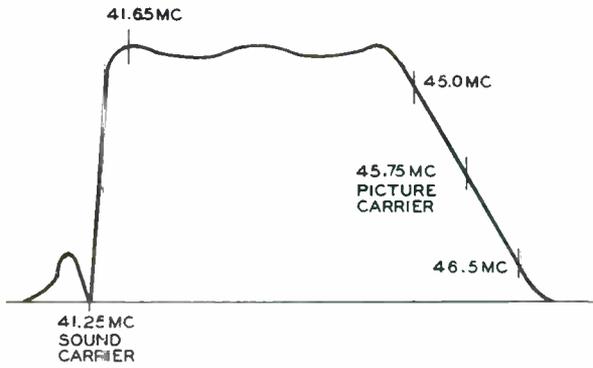


Fig. 4-7. Over-All Response of RF and IF Sections in RCA Victor Model CT-100.

This attenuation is provided through the use of traps. A bridged-T trap in the grid circuit of the first video IF amplifier provides the initial sound attenuation, which yields about the same 15 to 1 ratio of picture-to-sound carrier level that is employed in most intercarrier receivers. The use of the sound-level control in the resistive portion of the trap provides the necessary adjustment to obtain the desired ratio. Although bridged-T traps are not uncommon, the use of a variable resistance in connection with the trap in this part of the circuit is unusual. Before the sound IF carrier is further attenuated, it is taken off and fed to the sound IF detector. The take-off point is shown at the plate of the fifth video IF amplifier.

Preceding the video detector, a second bridged-T trap further attenuates the sound IF carrier. The adjustment procedure for this receiver specifies that the sound-rejection control should be adjusted for maximum attenuation of the sound IF signal. At this setting, an attenuation of 60 db below peak response is provided. Thus, the sound carrier is practically eliminated before the signal reaches the video detector.

The over-all IF response of the receiver from the mixer to the video detector conforms with the drawing in Fig. 4-7. Note that this response fulfills the bandpass

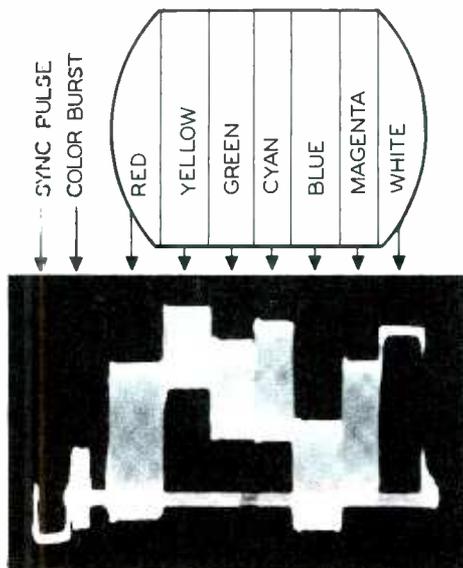


Fig. 4-8. Color-Bar Pattern and Associated Composite Color Signal at Output of Video Detector.

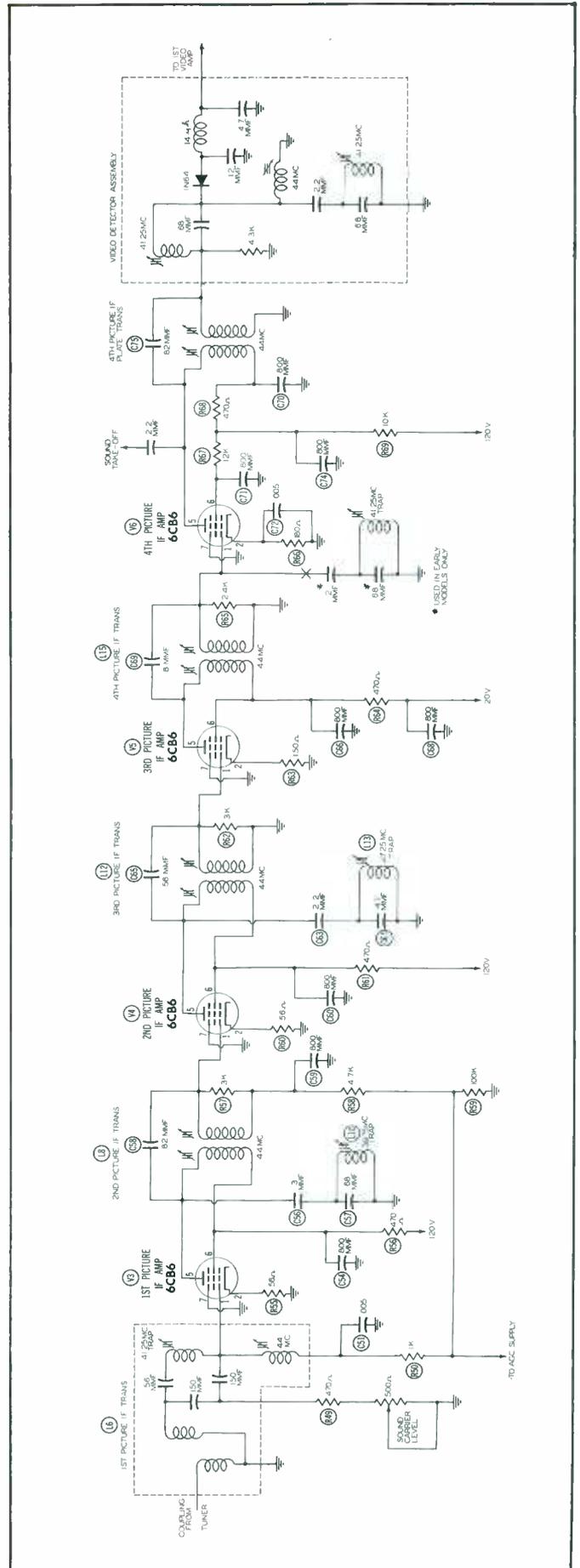
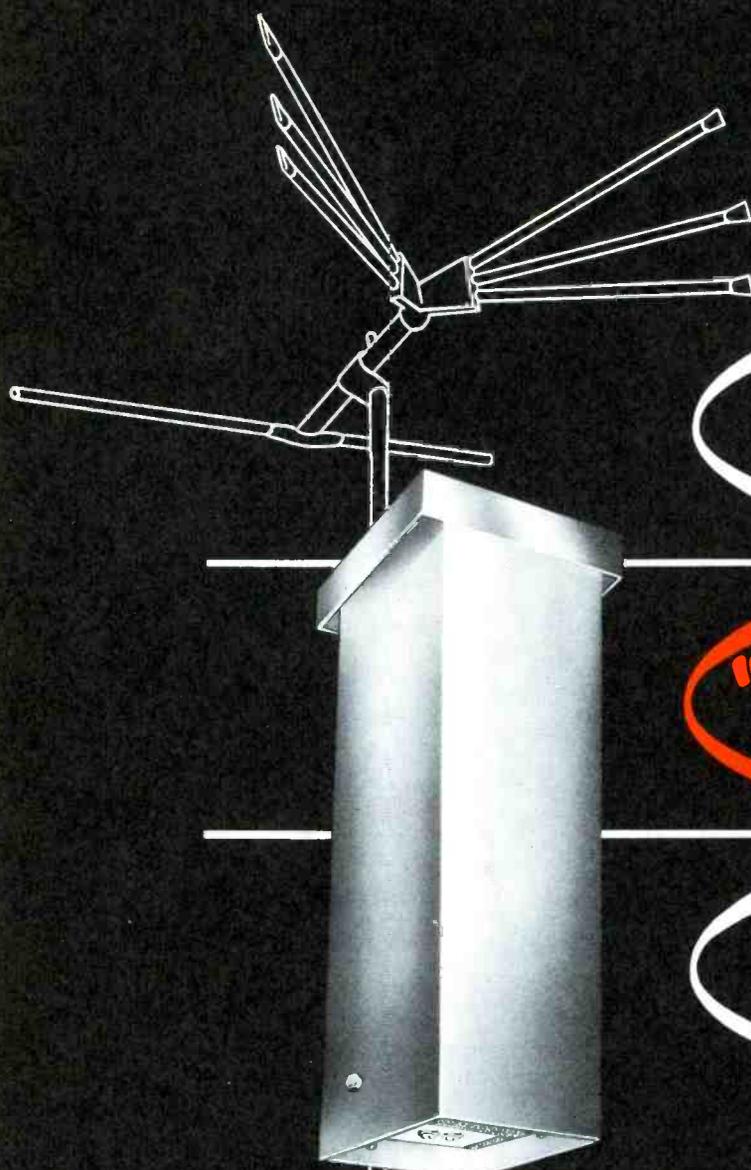


Fig. 4-9. Video IF and Detector Circuits in Westinghouse Model H840CK15.



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- **ANTENNA MOUNTED:**
for best signal-to-noise ratio even with long lead-ins.
- **SINGLE COAX CABLE:**
feeds 24 volt power up to "De-Snower," and strong clear signals down to receiver.
- **TWO MODELS:**
Channels 2-6, or 2-13. Flat response for color.

The only way to improve the performance of modern cascode tuner TV sets is to mount a *lower noise* cascode amplifier right at the antenna. This is the principle employed by Jerrold in designing head-end equipment for its famous community systems where as many as 5,000 sets are connected to a single antenna.

The Jerrold "De-Snow" is a broadband antenna-mounted preamplifier using low-noise 6BQ7-A's ahead of 6AK5 and 6CB6 tubes to provide a whopping 25 db gain on all VHF Channels. With this high output, shielded coax can advantageously be used to further reduce noise pick-up on the antenna lead. A Jerrold signal step-up transformer matches the 72 ohm coax to 300 ohm receiver inputs. This combination provides the cleanest "de-snowed" pictures attainable in any fringe area.

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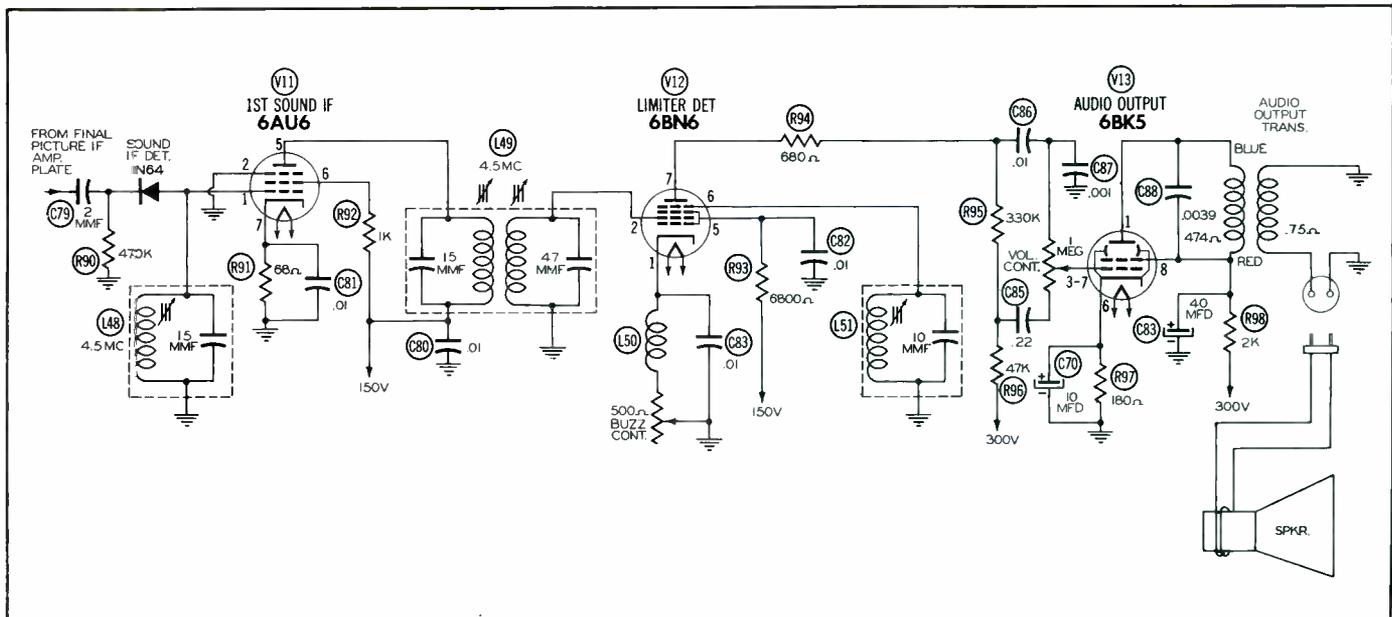


Fig. 4-10. Sound Circuits in Arvin Model 15-550 Color Receiver.

requirements for good color reproduction. These requirements are illustrated by the response curve shown in Fig. 4-5A.

An interesting design feature of the five-stage IF strip in Fig. 4-6 is the use of a 6CL6 as a fifth video IF amplifier. This tube is a power pentode which would not be used normally in this application. The signal level at the input of this stage is quite high, however; and this tube is used to provide the necessary signal-handling capabilities.

The video signals appearing at the output of the video detector consist of luminance, chrominance, horizontal and vertical sync pulses, and the color burst. The photograph reproduced in Fig. 4-8 shows the waveform of this output signal for the period of one horizontal line. The drawing above the waveform depicts the color-bar picture on the screen at the time the waveform was taken.

The RCA Victor Model CT-100 uses five stages of IF amplification as do models by several other manufacturers. Still other manufacturers have designed their color receivers with four IF stages. A partial schematic of the Westinghouse Model H840CK15 is presented in Fig. 4-9. Four 6CB6 pentodes are used; and except for the location of the sound take-off point and the numerous 41.25-mc traps, the circuitry is much like that used in many monochrome receivers.

Sound IF and Audio Sections

With the exception of the separate sound IF detector, the sound IF and audio sections of color receivers follow conventional monochrome design. If the reader knows the theory of intercarrier operation, he should have little difficulty in understanding and working with these sections in color receivers.

It has been mentioned that the sound IF carrier is severely attenuated in the video IF strip; consequently, the output of the video detector contains virtually no 4.5-mc beat signal. Sound information must be obtained from a point ahead of the video detector. This take-off point

is usually the output of the final video IF amplifier. The signals available at this point are in the IF range; and in order to obtain the 4.5-mc sound signal, a detector is necessary.

The sound IF and audio circuits used in the Arvin Model 15-550 can be seen in Fig. 4-10. A 1N64 crystal diode at the input of the first sound IF amplifier is used as the sound IF detector. The load impedance provided by L48 is tuned to 4.5 mc. Since the picture and sound IF carriers are the input signals, the action of the diode and its load results in the production of the 4.5-mc sound signal. From that point on, the sound information is handled as in monochrome receivers.

In the next issue, we will continue the discussion of the color receiver circuits which follow the video detector.

In order to give the reader an opportunity to test himself on the material in this issue, we are including a few questions that are answered in this discussion.

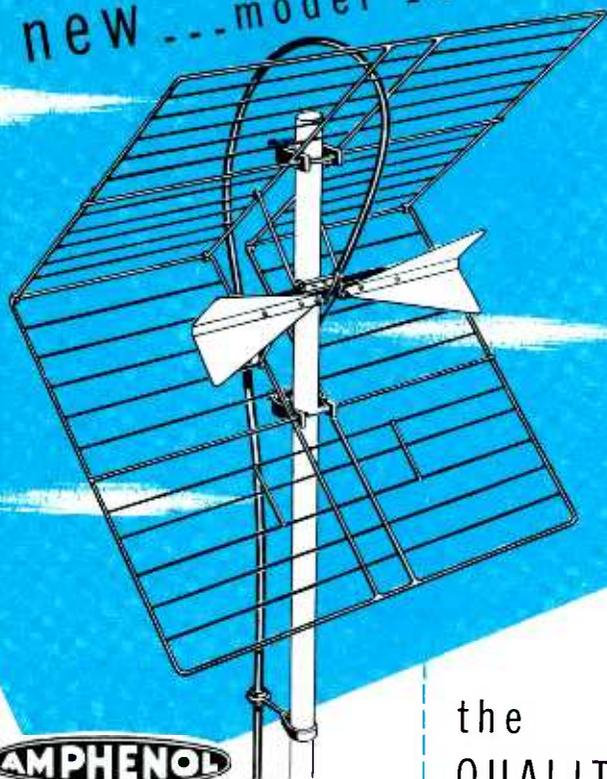
1. What is the basic requirement of a tuner which is used in a color receiver? Why?
2. What are the upper and lower bandpass limits of the video IF section in a color receiver? How does this compare with the IF response of an average black-and-white receiver?
3. Why is the sound IF carrier severely attenuated in the video IF section?
4. Why is a sound IF detector employed in a color receiver?

C. P. Oliphant

and

Verne M. Ray

new ... model 114-093



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The electrical characteristics of the new LIGHTWEIGHT Corner Reflector are excellent. The gain rises from 8 db to 12½ db across the UHF channels, more than enough gain to provide sharp, clear pictures in weak signal areas. Directivity, as on all AMPHENOL antennas, is exceptionally fine. There is one strong forward lobe that makes antenna/station alignment easy for the installer.

With the addition of the LIGHTWEIGHT Corner Reflector to the AMPHENOL line of quality antennas, AMPHENOL now offers every installer a quality choice of UHF Corner Reflectors—the new 114-093 LIGHTWEIGHT and the “king-size” model 114-058 Corner Reflector, previously in production.

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Dollar and Sense Servicing

(Continued from page 39)

SIDELINES. One neighbor of ours uses television to get her mending and ironing done. Seems as how darning of socks goes faster when she listens to some program and looks occasionally at the picture to give her eyes a rest from the cross-stitches.

Our own daughter writes letters to Australian Brownie Scouts or sews doll clothes while watching the daily dose of westerns and glances up at the screen only when the action becomes irresistible.

A Connecticut housewife paints in oils right in front of her TV set. According to columnist Jack Gould in the New York Times, she says, "You can get lots of painting done during the commercials. There are many programs where you don't miss anything by not watching them . . . Best for painting," she goes on to say, "are programs of the What's-My-Line type, where you can take a quick look at the guest contestant and go on about your work."

If painting in front of TV sets catches on, program producers will have a new challenge to meet. When you're trying to concentrate on something else, these working televiewers say, you're more conscious than ever of a bad program.

Thus is TV unwittingly meeting the criticism of die-hard radio fans that you can't work while you watch. And thus has this country taken one more revolutionary invention in its stride, for better rather than for worse.



SOUND. Professional quality of sound accompaniment for home movies, the goal of practically all 8-mm and 16-mm amateur enthusiasts, has until recently been too costly for all but a few. Magnetic striping on the back of developed film attracted interest but cost as much as 3 1/2 cents per foot, which is real money for a 400-foot reel that lasts about 20 minutes. Striping doesn't work out too well, either, because temperature and humidity often combine to crack off the coating and thus make the sound track noisy. Laminated striping cures this trouble; but its cost is still high, as also are projectors equipped for magnetic sound. Best hopes lie with a radically new approach to the sound problem.

An electronic control system now being patented by Eugene Anthony (formerly television and radio service manager for General Electric Supply Corp., in New York City) permits use of any standard two-track magnetic tape recorder and standard magnetic tape with any movie projector to achieve synchronized sound. No extra processing whatsoever is involved. Synchronization is always accurate to within the spacing between adjacent sprocket holes. The simple attachments required on the recorder and projector can be put on by a service technician in a few minutes and connected to the electronic control chassis. Installed cost of the control unit and accessories is expected to be about \$100.

The user feeds commentary and background recorded music conventionally to the microphone or other inputs of the recorder while watching the projected film. Control signals for controlling projector speed during playback are recorded automatically on the other track of the film. For lip synchronization of sounds recorded during filming, such as baby's first words or the scream of Aunt Nellie

as a spider is dropped down her neck, a simple sprocket-tooth switch device is added to the camera.



CLASSICAL. Don't comment disparagingly about high-brow music lovers, because they account for about 30 per cent of all records sold today. This means they buy at least that proportion of the phonographs sold, generally in the most expensive high-fidelity models, and they contribute more than that proportion to servicing income from audio amplifiers, radio-phonograph combinations, and phonographs.

The golden rule for success in servicing is — if you can't say something nice about a topic, don't say anything. You can never tell when a casual comment may offend and thereby cause loss of a customer.



HAUNTING. Sounds of footsteps going up and down stairs when nobody is there offer potential business to service technicians, according to Leo Connor in a recent issue of NRI's National Radio-TV News. To haunt stairways of recreation rooms, Leo says, you merely have to mount a solenoid-operated striker under each stair tread and connect them all up to contacts mounted on a motor-driven drum. By arranging contacts properly or providing an extra set of contacts, you can even make the ghost go halfway up the stairs and then come back down again at your call. The firm of Herbach and Rademan in Philadelphia is suggested as a source for the motor, solenoid coils, and plungers. For construction details, write editor Lou Menne at National Radio Institute in Washington and ask for a copy of his June-July 1954 issue.



INTERFERENCE. If you get auto-radio service job where conventional techniques fail to cut down ignition interference, try measuring continuity between the brass cap at the end of a spark-plug lead and the cable itself. In some new models of cars of a well-known make, as many as half of the spark-plug cables are open. The spark jumps across all right, so the performance of the car isn't noticeably poor; but what that spark does to operation of the auto radio equipment is really terrific. These caps are just crimped on, and

lately the crimp hasn't been deep enough to pierce the insulation and make contact with the inner conductor.



BANKS. Selling techniques of TV-radio dealers affect profits of banks, according to a speech by Pennsylvania banker W. F. Kelly before the National Association of Electrical Distributors. Dealers using high-pressure or unethical sales techniques were warned to improve their business practices if they expect banks to continue accepting their credit paper.

When people are rushed into buying something they can't afford or don't really want, they often neglect to make payments. The bank then has to send out men to collect or hire lawyers to force payment in court — both costly practices. Passing the buck to the banker is thus no way to stay in business. Much better is a good honest selling job using every persuasive technique given in books on salesmanship. Unfortunately, we know of no really good books written directly for TV and radio selling, so you'll have to translate the general recommendations yourself. Here's a wide-open field for a TV salesman to become an author.



REPORTING. Two TV sets in the news room of the New York Times were hooked up to automatic sound recorders while the sets were watched by reporters during the Army-McCarthy hearings this spring. Accurate quotes of the proceedings were thus obtained by playing back the sound recordings for incorporation in news stories that were set in type long before the actual text came over the news teletype wires conventionally. Other important news events are being covered more and more in this manner, so that TV sets are becoming an essential part of the modern newspaper office.



STRETCHER. We highly admire the shiny new Sylvania dolly for transporting TV chassis, but the question that keeps rumbling around in our head is: Should the "Corpse" go out head first or feet first?

JOHN MARKUS

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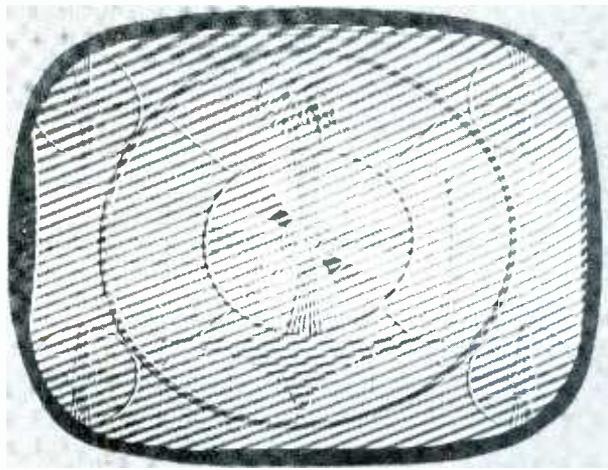


Fig. 7. A 28-Mc Beat Produced by Amateur Transmitter.

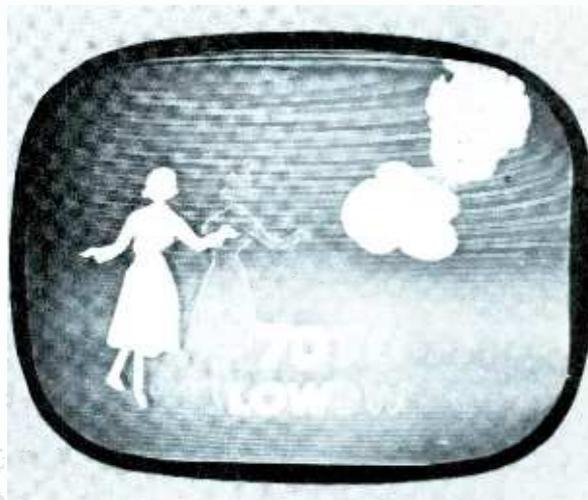


Fig. 10. Ghost Due to Reflected Signal.

be eliminated by the installation of a high-pass filter in the antenna-input circuit of the television receiver. This filter should be installed as close to the tuner as possible. Fig. 8 is the diagram of a typical high-pass filter. Any of the commercially available high-pass filters which are made for this purpose should be satisfactory.

The installation of a high-pass filter will eliminate any interference from the fundamental frequency on which an amateur may be operating. If the amateur's transmitting equipment should be generating harmonics, the installation of a high-pass filter will not correct the interference. In this case, the offending amateur should be notified that his equipment is radiating harmonics. Usually the amateur operator will cooperate and either not transmit when such transmissions might interfere with television, or he may take steps to

eliminate the harmonic radiation from his transmitter.

Fig. 9 is an illustration of interference from a small electric hand drill. This type of interference may also be caused by electric motors,

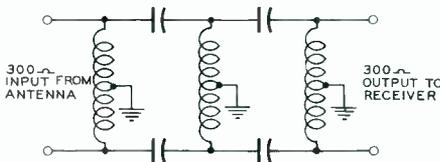


Fig. 8. A Typical High-Pass Filter.

fans, air-conditioning units, refrigerators, and other electrical appliances. The installation of commercially available line filters between the interfering device and the AC line or between the television set and the AC

line will do much toward eliminating this type of interference.

Fig. 10 is an illustration of ghosts due to signal reflections. A major characteristic of this type of interference is that the ghost does not change with a change of receiver tuning. In many cases, reorientation of the antenna will correct this trouble. If the ghost should still exist after reorientation of the antenna, it may be necessary to change the location of the antenna or the lead-in wire. Ghosts may also be caused, as in the case of a long lead-in wire, by improper matching at one or both ends of the antenna lead-in.

Fig. 11 is an illustration of interference caused by radiation from the local oscillator of another television receiver. This is a mild case of radiation. In some instances, radiation from the local oscillator of a

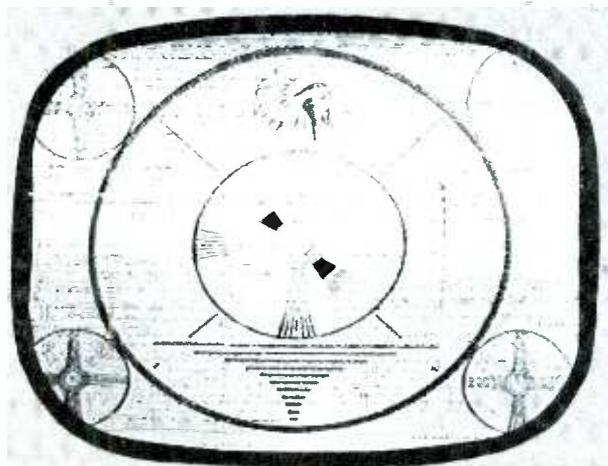


Fig. 9. Interference Caused by Small Electric Drill.

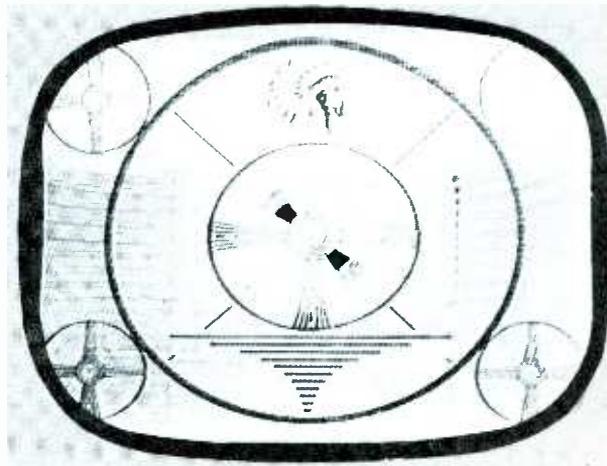
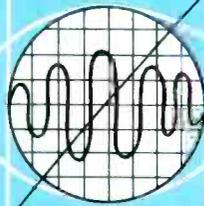


Fig. 11. Local-Oscillator Interference From Another TV Receiver.

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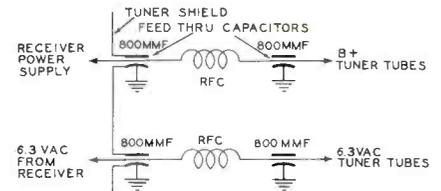


Fig. 12. Bypass System for the Power Leads to Tuner.

TV receiver is of sufficient amplitude to overload another nearby receiver. The safest cure for this type of interference is to find the offending receiver and by the use of approved methods to install a bandpass filter in its antenna-input circuit. This will prevent its antenna from radiating the interfering signal. It may be necessary to install a line filter between the receiver and the AC line. In some extreme cases, RF filter units should be installed in all power leads to the tuner. Fig. 12 is an example of the latter type of installation. If used along with the aforementioned antenna and line filters, the filter system in Fig. 12 will keep the oscillator radiations from charging the chassis and thus will keep the chassis from radiating.

Fig. 13 is an illustration of one type of diathermy interference. This is rather a mild case, and in most cases may be effectively eliminated by the installation of a high-pass filter at the antenna input and by the use of a line filter between the AC line and the TV receiver.

Some of the older types of diathermy and industrial heating equipment were built using little or no filtering in the power supply, and interference from these machines will show up with one or two black bars. Most of these old machines have been located, and steps have been taken to make them TVI proof.

Although this discussion may not have covered every type of interference, most of the principal kinds have been illustrated. The reader may recognize some of them from his past experience and may encounter new ones in his future servicing work. If the foregoing material can be used by him as an aid in diagnosing and curing interference problems, it will have served its purpose and well.

IN THE SHOP

Bench Picture Tube

After receiving many requests for information on setting up a picture tube for use on the bench, we decided to try one ourselves to see just what the problems were and what would be

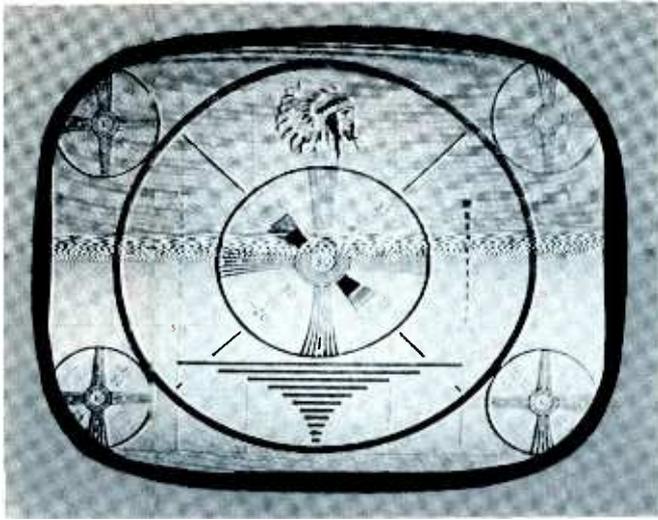


Fig. 13. One Type of Diathermy Interference.

That is an additional reason for including them as part of this bench setup. The most commonly encountered focus coils have the following ratings:

240 ohms (for use in circuits having approximately 200-ma drain),

360 ohms (for use in circuits having approximately 140-ma drain),

470 ohms (for use in circuits having approximately 100-ma drain),

1,000 ohms (for use in circuits having approximately 75-ma drain).

These coils will cover the large majority of applications; however, you may find it necessary to keep on hand one other type of focus coil, the combination electromagnet and permanent-magnet focus coil which seems to be gaining in popularity.

Fig. 14 illustrates a simple but functional method for mounting the test picture tube. The rear upright board is permanently mounted. The front tube rest is also attached to the base. After the picture tube is in position, the front piece with the safetyglass in it is put into place and attached with screws to the picture-tube rest. The diagonal brace is then put in place and held with screws to keep the front piece vertical.

On the rear of the base board can be seen a small chassis which contains a female octal socket. From four of the pins of this socket, wires run to four female pin sockets. Each yoke selected for this test setup is wired to a male socket which can be plugged into the socket on the small chassis. The pin jacks are coded so that they can be identified. Two sets of test leads are prepared for use with this arrangement. One set of leads has alligator clips; the other set contains pins for connecting to chassis which have plugs on their yokes.

It is not necessary to mount the deflection yokes on a bracket, for they will hold their position fairly well. However, the focus magnet must be mounted on a bracket, because it will move much too easily. The focus coils must likewise be mounted on brackets. The bracket which holds the focus magnet or focus coil can be mounted on a small board wide enough to prevent it from tipping over. This eliminates any need for fastening it to the base of the picture-tube mount.

Sync Separator and Amplifier

Because the sync section of a TV receiver can give rise to puzzling

needed. We came up with the following ideas and suggestions which we thought might be of interest. Although this setup may seem to be quite expensive, it will probably pay for itself in time saved. For instance, consider how long it takes to remove the picture tube from a cabinet when it is mounted separately. Another thought to consider is the ever-increasing size of picture tubes. They are becoming more and more difficult to handle safely — hence this is another point in favor of a test picture tube on the bench.

First of all, it must be understood that no one particular yoke can take the place of all types which are in use. In other words, there is no such thing as a completely universal yoke which will suffice for all applications. Therefore, the biggest problem is to determine what yokes should be used for this project.

The yokes selected must have inductances in the horizontal and vertical coils relatively close to the inductances required by the sets under test. Since most of the yokes in use have very nearly the same inductance (50 mh) in their vertical-deflection coils, principle concern should be given to the horizontal-deflection coils. Inductances in horizontal-deflection coils vary anywhere from about 8.5 mh to 30 mh. Therefore, if three 70-degree yokes

are selected with approximately 10-, 20-, and 30-mh inductances respectively, in the horizontal-deflection coils, they can be used with all the 70-degree sets except those sets using a low-inductance, vertical-deflection coil. The latter sets would necessitate the use of a yoke with a 30-mh horizontal coil and a 3.5-mh vertical coil.

Chassis which are used in sets employing 90-degree deflection systems will require a separate unit in order to obtain a proper raster for trouble shooting sweep circuits. At the present time, one 90-degree yoke will suffice for all the sets being manufactured for wide-angle deflection. This yoke should have approximately 12 mh in the horizontal coil and 45 mh in the vertical coil.

To service practically all the sets now in use, it is necessary to set up two picture tubes for bench use — one for 70-degree sets and one for the larger 90-degree sets. As stated before, this increases the cost of such a setup; but the arrangement will probably pay for itself in a short time if the shop has enough work to warrant its use.

Another item that this setup requires is about four focus coils for the sets that use them. Most of the sets which use focus coils incorporate them as a part of filter networks.

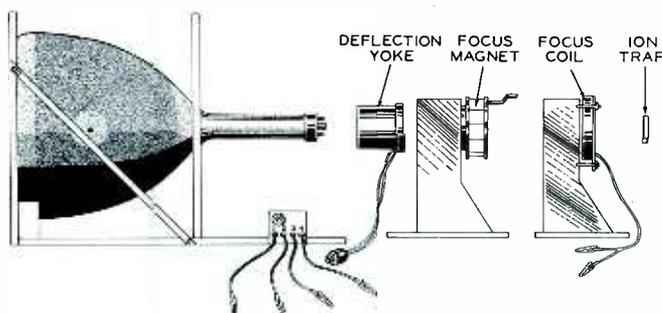
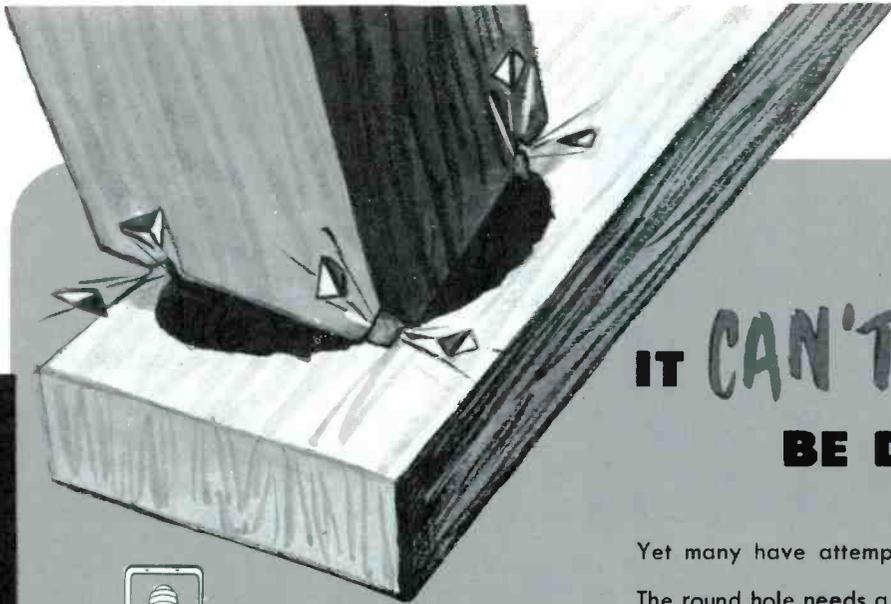


Fig. 14. Suggested Layout for a Bench Picture Tube.



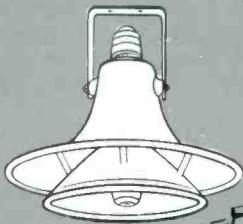
IT CAN'T BE DONE!

Yet many have attempted to try it.

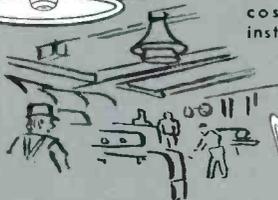
The round hole needs a round peg—custom-fit to meet the need. In the choice of a speaker, just as in the choice of the peg, the point of application should be the governing factor.

So why waste loudspeaker capacity and amplifier power using the wrong speaker for the job? University makes available over 50 different models of speakers, each designed to meet a particular requirement most efficiently. University loudspeakers are *application engineered* to provide optimum performance with maximum economy—technically and cost-wise.

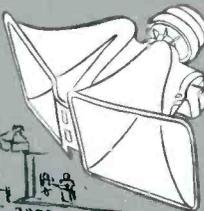
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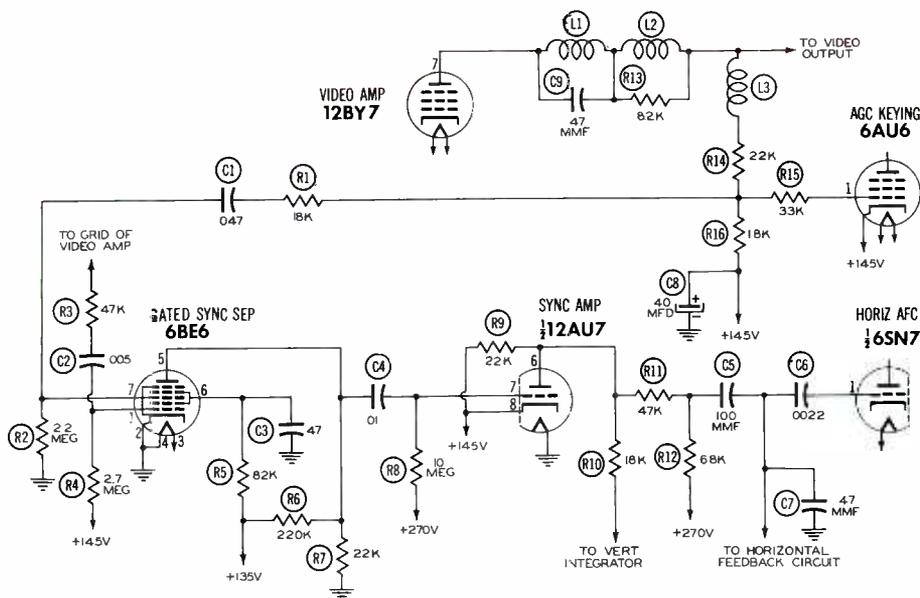


Fig. 15. Partial Schematic Diagram of Receiver Discussed in Text.

symptoms if troubles occur in it, we are presenting in narrative form a few typical problems and their solutions. A partial schematic of the receiver which we are using as a reference is shown in Fig. 15.

Problem No. 1.

The picture in the set had a twitch and waviness which appeared to be caused by incomplete action of the sync separator. The technician suspected that there was video in the sync signal arriving at the AFC circuit and that the presence of this video was causing improper action of the circuit.

In order to prove or disprove this theory, the scope lead was placed on the plate lug of the sync separator and the waveform was observed. There were two things wrong with the signal. A great deal of video signal was present, and the amplitude of the waveform was much lower than it should have been. Instead of the eight-volt peak-to-peak signal required, there were only two and a half volts.

Next, the signals were checked at the two input grids (pins Nos. 1 and 7) of the sync separator. The waveforms of these signals proved to be proper in form as well as in amplitude. As a result of these indications (weak signals on the plate and correct signals on the grids), voltage checks were undertaken on the basis that the loss of gain was probably caused by incorrect operating voltages. A vacuum-tube voltmeter was used for the checks. All measurements were satisfactory except the plate voltage which measured 13 volts instead of

the 9 volts called for in the service literature.

An open screen-bypass capacitor could cause a loss of gain; therefore, the next step was to check C3. The quickest and easiest method to do this is by checking the screen with a scope. If there is a strong signal present, the capacitor is probably open. Bridging the capacitor with a new one would be the final check. When the technician investigated capacitor C3, he found that it was open; and after replacement of this capacitor, the set functioned normally.

Notice that the technician deserted his scope in favor of his voltmeter at one point in this troubleshooting procedure. Actually, he could have found the source of trouble more quickly if he had continued using his scope to check screen waveform while he was conducting his preliminary tests.

Problem No. 2.

This problem proved to be not only very interesting but quite puzzling as well. The set would not lock in horizontally and was very difficult to stabilize vertically. With everything considered, this indicated a loss of sync. However, when the scope lead was placed on the plate of the sync amplifier, a signal was found. This signal was not too good — besides being somewhat distorted, it was reduced considerably in amplitude. The signal on the grid was then checked on the scope and found to be good in both shape and amplitude. This indicated that the tube might be operating on improper voltages.

Therefore, the VTVM was used to measure the grid, plate, and cathode voltages. These voltages all seemed to be satisfactory. By this time, the technician was completely nonplused and decided that perhaps there was something wrong in the plate circuit of the sync amplifier and that whatever it was was having a very strong effect on the signal but not on the DC voltage. Hence, every component in the plate circuit was then checked with an ohmmeter and a capacitor checker. Still, nothing could be found defective.

The technician decided to back-track, so he applied the scope lead once again to the plate of the sync amplifier. Then came the realization that a gross error had been made. Subconsciously, the technician had accepted what he had seen on the scope as being the horizontal sync pulses; but on this second check, he noted the frequency of the scope and saw that it was set for 30 cps instead of for 7,875 cps!

A quick look at the schematic then brought about the conclusion that the signal being seen on the scope was undoubtedly being fed back from the vertical oscillator; therefore, the next step was to disable the vertical oscillator by grounding the grid and to turn down the brightness so that the picture tube would not be damaged.

With the vertical oscillator disabled, the sync-amplifier plate was again checked on the oscilloscope. Not a sign of a signal of any kind was present.

Putting all the facts together brought about the only possible answer to the question. Either the cathode was open between the socket and the actual element or the plate circuit was open in a like manner, since both the cathode and plate voltages at the socket were measured and found satisfactory. Therefore, two more tubes were tried. When these failed to help, the socket was examined and found to have a great deal of corrosion in the cathode pin socket. It was cleaned out by inserting a sharp-ended wire to scrape the corrosion loose, and it was then washed with carbon tetrachloride to remove any loose particles. After the vertical oscillator was restored to operation, the set operated normally.

The stumbling block in this trouble-shooting experience arose from a misinterpretation of a scope waveform. The moral is: check test equipment before and during its use to guard against such mistakes.



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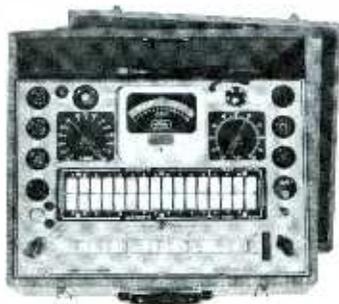
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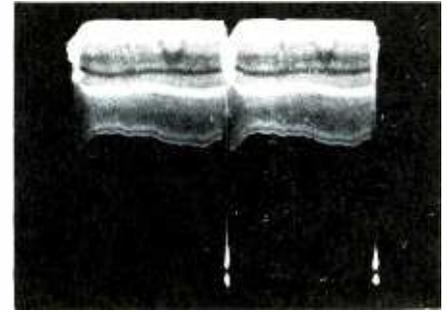


Fig. 16. Normal Signal on Plate of Sync Separator.

Problem No. 3.

A loss of sync was the first symptom noticed in the receiver. When the horizontal- and vertical-hold controls were manipulated, the picture stood still long enough that one could see what it looked like; but the picture was not completely locked in. In addition, the picture had too much contrast and appeared to be slightly negative.

From these symptoms, the conclusion was drawn that there were at least two and maybe even three stages being affected by the trouble. These stages were the video amplifier (because of the strong contrast), the sync separator and amplifier (because of no sync), and the AGC (because it could cause either excessive contrast and sync loss or both).

Since the lack of sync was the first thing noticed, the sync section was considered a good place to start checking. So, the scope probe was first placed on the plate of the sync separator. Instead of finding a normal waveform resembling that of Fig. 16, one that was more like that of Fig. 17 was found.

This excessively distorted output indicated that the signal was probably being distorted at the separator; hence, voltage readings were taken. The voltage on pin No. 7 of the sync separator (see Fig. 15) was

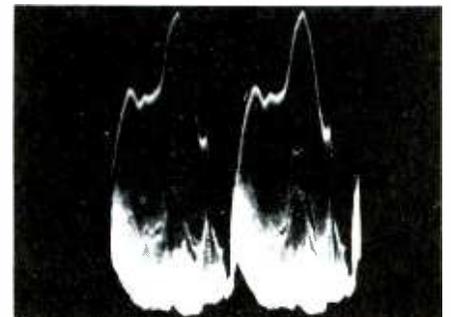


Fig. 17. Signal on Plate of Sync Separator With Leaky Input Coupling Capacitor.

greatly out of proportion. Instead of measuring -0.5 volts, it measured +2 volts. This positive grid voltage indicated that the coupling capacitor C1 probably was leaky. A continuity check with an ohmmeter soon substantiated this theory with a reading of 220,000 ohms.

Since the leakage resistance in the coupling capacitor together with resistors R16, R1, and R2 forms a voltage-divider network and since the bias on the AGC tube is tapped from this network, the bias was affected by the leaky capacitor. This caused a change in the output of the AGC tube and a resulting overload condition in the RF circuits of the receiver. Hence, a negative picture was produced as one of the symptoms.

Problem No. 4.

Once in a while a technician can be lucky and have an easy job of locating a trouble. This was one of those times. The symptom was a complete loss of horizontal sync. Vertical sync was apparently good. A new AFC tube and an oscillator tube were tried, but to no avail.

The trouble was somewhere after the take-off point for the vertical sync, since the vertical sync was all right. Accordingly, the first checks were made in the horizontal oscillator and AFC circuits with an oscilloscope. The waveforms on the oscillator were satisfactory; however, when the scope lead was moved to the grid of the AFC tube, no signal was found.

One of three items could be at fault and cause this. C5 or C6 could be open and thereby interrupt the signal, or C7 could be shorted and thereby ground the signal. The scope lead was moved to the junction of C5, C6, and C7; still there was no signal. A check with the ohmmeter soon disclosed that the signal was not being grounded by a short in C7. A scope check at the junction of R11 and R12 showed the presence of a signal; so capacitor C5 was replaced, and the set resumed normal operation.

The tests in this problem were so simple and straightforward that much less time was needed to make them than to tell about them. If all TV troubles were found this easily, there would be fewer discouraged service technicians.

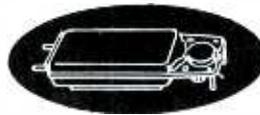
Problem No. 5.

Here was one of those jobs that make technicians "tear their hair." The symptoms were confusing. The set had horizontal tearing the pulling;

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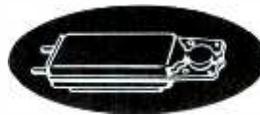


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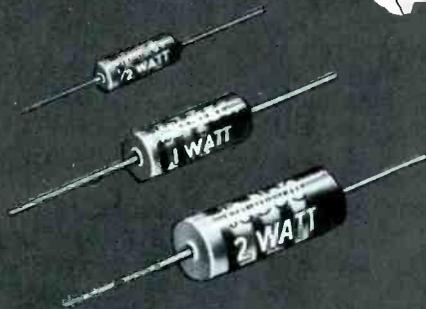
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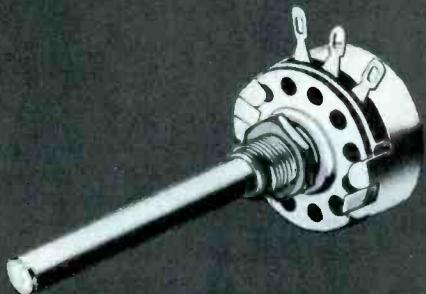
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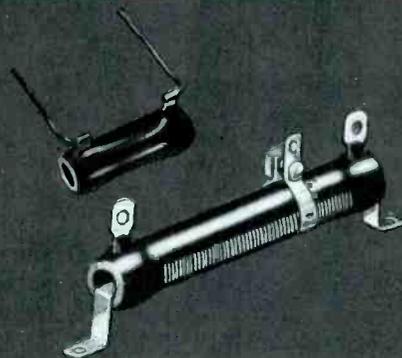
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and when new tubes were tried in the sync, AGC, and horizontal-oscillator sections, they were of no help. When the contrast control was turned up, a Christmas-tree effect would occur in the picture.

With these facts to go on, it was apparent that the amplitude of the video in the output circuit was affecting the operation of the oscillator or the AGC in some manner. In order for this to occur, it was probable that the video was getting into the AFC circuit or into the oscillator in some way. First, the scope lead was placed on the horizontal-oscillator coil. The waveform appeared to be normal. The input of the AFC circuit was checked with the scope and showed considerable distortion. The plate of the sync amplifier was then checked, and some video signal was noted. Next, the grid waveform of the sync amplifier was checked and found to be clean. As a matter of course, the scope lead was then placed on the cathode of the sync amplifier where a very strong video signal was seen.

An examination of the circuit schematic showed that the cathode of the sync amplifier was connected to the 145-volt line. Since the filter capacitor C8 was the only filter in this line and since the video output tube was supplied from this line, the technician reasoned that a logical suspect was the filter capacitor C8. If this capacitor opened, there would be no filtering of the video signal which was developed in the plate circuit of the video output tube. A check of capacitor C8 confirmed the fact that it was open; and upon replacement of this component, the set functioned properly.

The oscilloscope proved to be an invaluable aid to the technician in each of these problems. Remember its usefulness the next time you encounter troubles in the sync amplifier and separator.

Figs. 4, 5, 6, and 10 were taken from telecasts by WFBM-TV, Indianapolis, Indiana. The pictures do not in any way reflect upon the quality of the transmitted signal, since all picture defects were introduced at the receiving site. We wish to express our thanks to WFBM-TV for permitting us to use these photographs.

Henry A. Carter and
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Examining Design Features

(Continued from page 37)

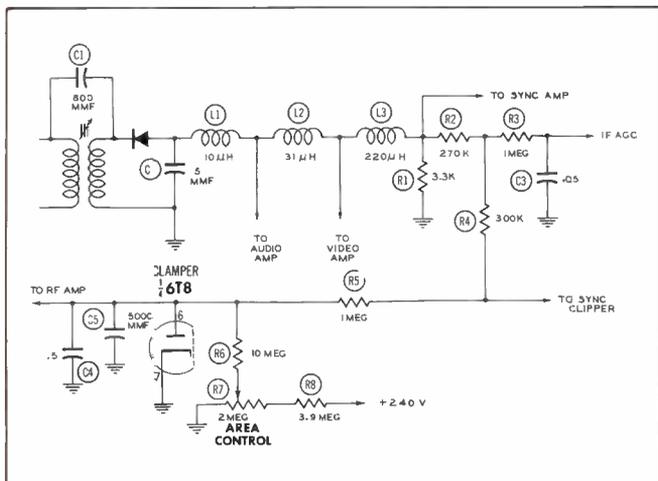


Fig. 2. The Circuit Which Provides the Tuner AGC Voltage in the General Electric Model 21C240.

circuit also contains the brightness control.

Sound

The sound take-off point is located at the output of the video detector. The signal from this point is coupled to the grid circuit of the sound IF amplifier which consists of the pentode section of a 6U8. The amplified signal is then fed to the 6A6 limited by a 4.5-megacycle IF transformer.

Detection is accomplished by a conventional ratio detector employing two diode sections of a 6T8. The resultant audio signal is RC coupled to the grid of the audio amplifier which is the triode section of the 6T8. The setting of the volume control determines the level of signal applied to the latter stage.

A 6V6GT and its associated components constitute a conventional audio output stage.

AGC

The output of the video detector serves as the source of AGC voltage in this receiver. The detector output is filtered and isolated before being applied to the grids of the IF amplifiers. The AGC voltage that is applied to the RF amplifier is controlled by the circuit shown in Fig. 2.

A positive bucking voltage is applied to the tuner AGC line by the voltage-divider network consisting of resistor R8 and potentiometer R7. The potentiometer is termed the "area control" and serves to set the level

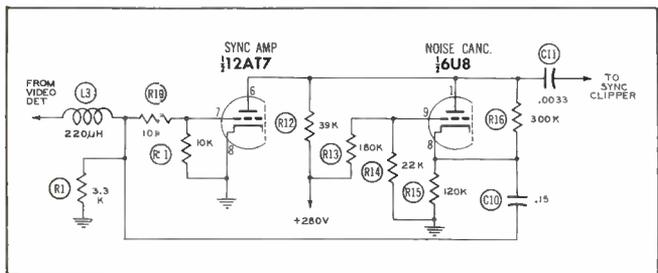


Fig. 3. A Schematic of the Noise-Cancellation Circuit in the General Electric Model 21C240.

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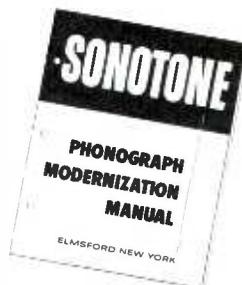
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of the bucking voltage. A clamper on the AGC line prevents the potential from becoming positive.

A switch ganged to the area-control potentiometer is normally closed. In the case of a very strong signal, the area control may be rotated toward the strong position until the switch is actuated. The switch opens and removes the B+ voltage from the RF amplifier. The strong signal is then coupled through the RF stage by the interelectrode capacitance of the tube, and the inoperative tube functions very much like an attenuator.

Sync

As shown in Fig. 3, a composite video signal of negative polarity is fed from the video detector to the grid of the sync amplifier. A negative signal is also fed to the cathode of the noise-cancellation tube through capacitor C10. A positive bias is applied to the cathode by the action of resistors R12, R16, and R15. A positive potential is also applied to the grid of this stage by the divider formed by resistors R13 and R14. The combined effect of these two voltages is to keep the noise-cancellation tube normally cut off. This stage does not affect the operation of the sync amplifier under these conditions.

When a strong noise pulse appears in the video signal, it is sufficient to overcome the bias on the noise-cancellation tube and the tube conducts. The result is a negative-going signal at the plate. This signal cancels the positive signal appearing at the plate of the sync amplifier. A "hole" then appears in the signal from the sync amplifier for the duration of the noise pulse. By this means, the strong noise pulses are prevented from being fed to the sync clipper and false triggering of the sweep circuits is avoided.

The composite signal from the output of the sync amplifier is coupled to the grid of a sync clipper. This stage employs one triode section of a 12AT7. A small negative bias is supplied to the grid from the AGC line.

The sync signals occurring in the plate circuit of the sync clipper are fed to the grid of a phase splitter. This stage uses a triode section of a 12AU7. The sync signals from the plate of the phase splitter are fed to an integrator network and then to the vertical-sweep section. The signals from the cathode of the phase splitter are coupled to the horizontal phase detector.

Vertical Sweep

The sync signal occurring at the plate of the phase splitter is fed

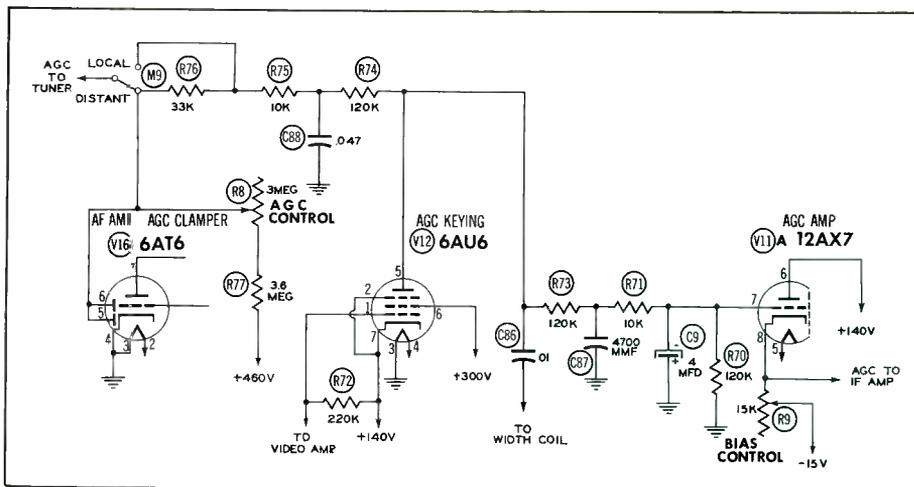


Fig. 4. A Schematic of the AGC System in the Arvin Chassis TE-340-1, -2.

through an integrating network and then to the grid of the vertical multivibrator, which is composed of the two triode sections in a 6BX7GT. The vertical-linearity control and the vertical-hold control are located in the cathode circuits of the 6BX7GT. The vertical-size control is contained in the plate circuit of one of the triode sections. The use of a 6BX7GT as the vertical multivibrator permits the elimination of a separate vertical-output tube because sufficient sweep output is available directly from the multivibrator.

Horizontal Sweep

The triode section of a 12AU7 functions as the horizontal phase detector in this receiver. A sync pulse from the phase splitter and a sample waveform from the horizontal-sweep output are fed to this stage. The phases of these two signals are compared, and any difference results in an error voltage. The error voltage is then coupled to the horizontal multivibrator to correct its frequency.

A positive potential is applied to the grid of the horizontal multivibrator by a voltage-divider network. The level of this voltage establishes the frequency of the multivibrator and is determined by the setting of the horizontal-hold control.

Two triode sections of a 12AT7 are connected as a cathode-coupled multivibrator to produce the horizontal-sweep signal. The horizontal-stabilization control serves as an adjustable ringing coil in the multivibrator circuitry.

The output of the horizontal multivibrator is coupled to the grid of the 6BQ6GT horizontal-output tube. There are two additional adjustments provided in the horizontal-sweep section. These adjustments are for width and for horizontal linearity.

There are two additional tubes associated with the horizontal section. For high-voltage rectification, a 1B3GT is used. The remaining tube is the 6AX4GT damper.

Low-Voltage Power Supply

The low-voltage power supply includes two 5U4G tubes to provide the necessary current by full-wave rectification. The inclusion of several dropping resistors in the output of the power supply provides the wide variety of voltages required for proper operation of the receiver. There are six voltage sources obtained in this way.

The primary winding of the power transformer has two possible connections. One is for a line voltage of 110 volts, and the other is for 117 volts. The selection of the desired connection is accomplished by placing the line fuse in either of the two fuse clips on the receiver.

UHF

There are three types of UHF tuners supplied with this line of receivers. Two of the tuners, RUX-001 and RUX-006/007, are single-conversion units. They both utilize a 6AF4 as the oscillator and a 1N82A crystal diode as the mixer.

The third type of tuner employs the double-conversion principle. In addition to the 6AF4 oscillator and the 1N82A mixer, a 6BK7A is included to act as a two-stage IF amplifier.

AGC SYSTEM IN ARVIN CHASSIS TE-340-1, -2

Strong noise pulses that are present in the video signal of a television receiver result in the appearance of black dots in the picture. These black dots are usually accompanied by white streaks immediately

after them. The reason for this phenomenon is that the coupling capacitors in the IF stages become heavily charged by a strong noise pulse. Since the grid circuits normally have a high impedance to ground, the charges do not leak off immediately and may cause the white streaks to appear.

Some of the recent Arvin receivers have incorporated a circuit designed to minimize these annoying white streaks. A schematic of this circuit, as contained in Arvin chassis TE-340-1, -2, appears in Fig. 4.

A 6AU6 is utilized in a conventional keyed AGC system to develop the necessary AGC voltage. This voltage is fed to the tuner in a straightforward circuit containing a Local-Distant switch and an AGC clamper. The clamper uses the diode sections of a 6AT6.

The departure from the normal circuitry is found in the method of feeding the AGC voltage to the IF stages. This is done by using a cathode follower. The triode section of a 12AX7 is used for this application.

By reference to the schematic diagram, it may be seen that the full AGC voltage is developed across resistors R73, R71, and R70. The grid of the cathode follower is connected to the junction of resistors R71 and R70. The voltage on this grid is dependent upon the AGC voltage. Bias on the stage is determined by the setting of the bias control R9. The arm of this control is returned to a negative potential.

The AGC voltage for the IF stages is taken directly from the cathode of the cathode follower V11A. As the AGC voltage becomes more negative, the cathode also becomes more negative. Since the potential of the cathode follows in step with the AGC voltage, the IF stages are effectively controlled by this voltage.

When strong noise pulses charge the coupling capacitors of the IF stages, the capacitors may become quickly discharged through the low-impedance offered by the cathode circuit of V11A. The quick discharge of the coupling capacitor minimizes the formation of the white streaks that follow the black dots caused by noise pulses.

Don R. Howe

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Traps for Standard Coil Tuners

(Continued from page 23)

In the Standard Coil tuner, the antenna-input circuit for each channel is contained on a separate strip. A schematic of this setup appears in Fig. 2. These strips provide a logical location for a trap. Since any one strip is connected to the circuit only when the set is tuned to a particular channel, the trap would also be in the circuit on only one channel. This would entirely eliminate the need for an additional switch. Another distinct advantage is offered by the use of this method. The series trap is connected directly across the antenna coil, terminals Nos. 8 and 10; consequently, there is no lead-in after the trap. A potential source of interference pickup is thereby eliminated. This complies with one of the previously mentioned criteria for trap installations.

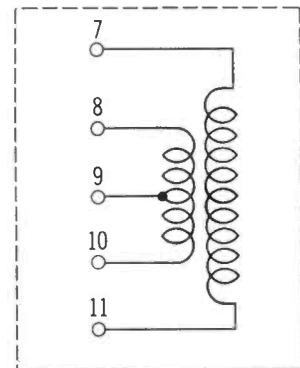


Fig. 2. Schematic Diagram of an Antenna Strip From a Standard Coil Tuner.

Several problems, both mechanical and electrical, arise because of the small space that is available inside the tuner. These problems are minimized, however, by a careful selection of component parts for the trap. Mounting of the trap is facilitated by the use of the strip terminals as tie points. The coil and capacitor which make up the trap may be soldered directly to these points. The trap then becomes self-supporting, and the physical mounting is easily accomplished and does not constitute a serious problem. Since the indi-

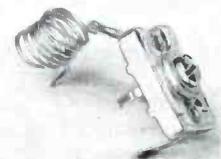


Fig. 3. A Series Trap Before Installation on a Strip.



Fig. 4. A Series Trap Installed on an Antenna Strip.

vidual strips are easily removed, the mounting may be done without working in the confined space of the tuner.

The capacitor selected for use in the trap is of the trimmer type. The maximum capacitance of the trimmer should not exceed 30 mmf. A maximum value of 10 mmf may prove more practical in many cases. The larger capacitors cover a wider band of frequencies but are more critical in their adjustment. Although a capacitor of lower value covers a smaller range of frequencies, it is more easily adjusted to remove the interference. It is therefore advisable to select as small a value of capacitor as possible when constructing a trap. If a capacitor of more than 30 mmf is selected, there is a danger of some shunting effect at the higher frequencies.

The inductance may be wound so that it will be resonant at the desired frequency when used with the selected capacitor. Because of the available space in the tuner, the length of this coil should not exceed 1/2 inch. When the trap is to be used at frequencies below 95 megacycles, a diameter of 3/8 inch is suggested. If the trap is to be tuned to a frequency higher than 95 megacycles, a diameter of 1/4 inch is a good choice. Fig. 3 shows a typical trap before it is attached to a strip.

Any combination of inductance and capacitance may be used, provided

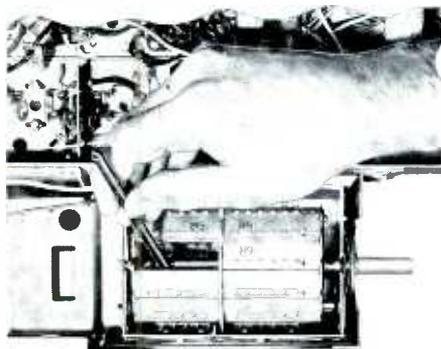


Fig. 5. Making a Tuning Adjustment on a Trap.

TABLE I

RECOMMENDED SPECIFICATIONS FOR TRAPS

Frequency Range (mc)	Capacitor (mmf)	Coil		
		No. of Turns	Diameter (inches)	Length (inches)
120 to 243	1.5 to 10	5	1/4	3/8
106 to 216	1.5 to 10	5	1/4	1/4
94 to 185	1.5 to 10	7	1/4	1/2
88 to 170	1.5 to 10	7	1/4	5/16
66 to 123	1.5 to 10	7	3/8	1/2
71 to 178	2 to 20	7	3/8	7/16
60 to 176	2 to 20	7	3/8	3/8
50 to 178	2 to 30	7	3/8	7/16

that the components resonate at the frequency of the interfering signal and that they are of the proper physical size. Some practical combinations are shown in Table I.

Before installing the trap on the strip, it is advisable to check the frequency range. This is done by temporarily connecting the coil and capacitor in a parallel-resonant circuit and by employing a grid-dip meter to determine its resonant frequency. Although this step is not essential, it may eliminate a time-consuming trial-and-error procedure.

When the coil is permanently affixed to the strip, it should be installed so that its axis is perpendicular to the axis of the antenna coils on the strip. This method of mounting minimizes the mutual coupling that may exist between the coils and results in a more satisfactory performance of the trap.

One end of the coil is soldered directly to terminal No. 8 of the antenna strip. The other end of the coil is soldered to one lead of the trimmer capacitor. The other lead of the trimmer is soldered to terminal No. 10. A trap is shown installed on an antenna strip in Fig. 4.

The capacitor should be tilted slightly when it is mounted. This permits tuning adjustments to be made without the shaft, which extends through the tuner being in the way of the alignment tool.

After installing the strip and the trap in the tuner, it is necessary to tune the trap. This is accomplished by utilizing the following procedure. One or two strips opposite the trap are removed, thus providing access to the trimmer capacitor. The receiver should be turned on and tuned

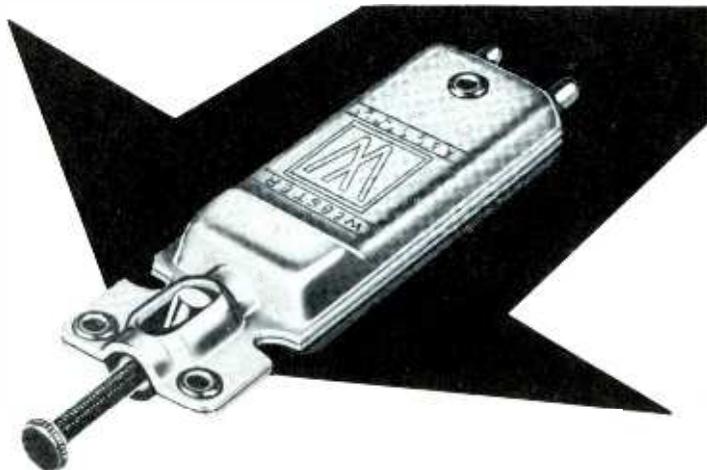
to the channel where the trap is installed. An alignment tool is then inserted through the opening provided by removing the strips. The trimmer is adjusted for an indication of minimum interference. Fig. 5 shows how this adjustment is made.

Before making this adjustment, it is often convenient to set the trimmer at maximum capacity. This permits the lowest frequency of the trap to be used as a starting point. A reference is established in this manner, and the operator can identify the point or points at which the trap is effective in eliminating the interference. If more than one point is found, the trap should be set at the point where maximum results are obtained. If necessary, a small degree of tuning is possible by adjusting the over-all length of the trap coil. If the coil is compressed to lower the frequency, care should be taken that none of the turns are shorted.

After the tuning adjustments have been made, the response curve of the channel should be observed. This may be done by using a sweep generator and an oscilloscope connected in the same manner as for visual alignment of the tuner. This check assures that the trap will not result in inferior performance on the channel containing the trap. At this time, the adjacent channels should also be checked to make certain that the trap has not affected them.

Installation of a trap in a tuner is not a panacea for all problems of television interference. It does, however, satisfy a definite need in several types of interference. A trap of this kind is not difficult to construct or install, and the results are very satisfactory.

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Notes on Test Equipment

(Continued from page 19)

fect by the technician himself, but replacement of some components in complex circuits may make it necessary to return the instrument to the manufacturer for realignment or adjustment.

The actual time spent in making such repairs and in routine maintenance would be only a small percentage of the useful life of the equipment, and so we believe that the technician is in no danger of eventually devoting all his attention to his test equipment to the exclusion of his service work.

It would be difficult to set an actual figure for the expected life of any test instrument. Short of actually being demolished through accident, test instruments can be kept operating with minor repairs until the service technician feels that they should be replaced with equipment of more recent design. Consider a multimeter, for example. The ohmmeter battery needs replacement only after a long period of time; switch contacts might possibly wear and need replacement; perhaps the greatest repair required would be the replacement of a burnt-out meter movement. After these repairs, the meter should function as well as a new one; therefore, the expected life of this type of instrument is very long indeed. Actual mechanical wear in any test instrument would be restricted to moving parts such as switches, dial drive mechanisms, sweep-generator drives, and attenuators. These can be replaced at much less cost than that of a new instrument. The result is that the instrument itself can hardly be considered to wear out; but it may be retired in favor of a newer design, as was previously stated.

One factor in determining the number of test instruments that a technician may acquire is a more or less natural aversion to tackling something strange, as he might be required to do when learning to operate a new instrument. The array of knobs, meters, and switches which appear on some instruments may actually be dismaying to some. However, the reverse can also be true inasmuch as many persons welcome the opportunity to work with a new instrument; and the more adjustments it has, the more intrigued they become.

Simplicity of operation is a virtue, but the usefulness of the instrument should not be sacrificed in the interest of simplified operation.

Our association with test instruments has given us a healthy

respect for the performance of modern high quality equipment. All things considered, we would be inclined to make the following recommendations: select your equipment with care and get as much as your space and budget will stand. In the last analysis, the test instrument is a tool; and the better a workman's tools, the better he can render his services.

The Hickok 655XC Color-Bar Generator

The new Hickok 655XC color-bar generator provides a wide variety of color signals suitable for checking, adjusting, and servicing color receivers. The horizontal-line frequency, the sound intermediate frequency, and the color-subcarrier frequency are all crystal controlled thus insuring utmost accuracy of these important functions. A photograph of this instrument appears in Fig. 1. The RF carrier may be conveniently set to either of channels 4, 5, or 6 with the aid of a crystal-controlled calibrator such as the Hickok Model 690.

The following output signals are available at connectors on top of the chassis: video (with either positive or negative polarity), RF, and 3.58-mc signals.

A function selector switch permits selection of three types of color-bar patterns, all with colors that are 100-per-cent saturated. These are: (1) a 5-bar pattern containing green, yellow, red, magenta, and blue bars; (2) two bars produced by positive signals on the I and Q axes; and (3) two bars produced by positive signals on the R - Y and B - Y axes. This choice



Fig. 1. The Hickok 655XC Color-Bar Generator.

of signals makes the instrument extremely suitable for checking receivers of either the I and Q type or the R - Y and B - Y type.

A number of other control switches are provided and have the following functions:

POWER	Turns the power on or off.
MOD	Applies modulation to RF carrier, depending upon the setting of other switches.
SOUND	Applies unmodulated sound carrier to signal.
Y	Applies the Y or luminance component to the signal.
CHROMA	Applies color modulation to the signal.
I and R - Y	Applies I or R - Y component to the signal, depending upon the setting of the function-selector switch.
Q and B - Y	Applies Q or B - Y component to the signal, depending upon the setting of the function-selector switch.
VIDEO POLARITY	Allows choice of either positive or negative polarity of the video signal available at video-output connector or as modulation to the RF signal.

In addition, a variable attenuator controls the amplitude of the video signal at the video-output connector but does not control the video modulation of the RF signal. An RF attenuator controls the amplitude of the RF signal.

Eighteen tubes are used and include the following types:

- 1 - 5U4G
- 1 - 6BJ7
- 4 - 6U8
- 5 - 12AT7
- 4 - 12AU7
- 3 - 12AV7

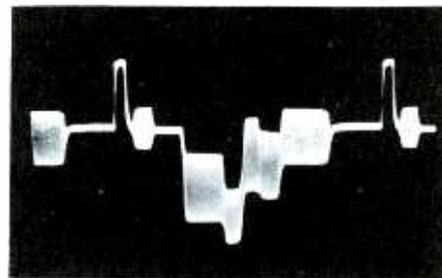


Fig. 2. Video Output Signal of the Hickok 655XC With Control Switches Set for Five-Color-Bar Pattern. The Signal Has Positive Polarity.

The instrument is housed in an attractive carrying case with a removable lid.

Several photographs of waveforms were taken to show the variety of signals available and the manner in which some were used in our laboratories for checking and adjusting a color receiver. Figs. 2 through 7 are the results of applying the video output directly to a wide-band oscilloscope. Fig. 2 is the video-output signal of positive polarity with the function-selector switch set for the five-bar pattern. At the left, the narrow peak appearing above the axis is the horizontal sync pulse followed immediately on the right by the color burst. The next pulse to the right is the signal which represents the green bar; and the succeeding pulses are for the yellow, red, magenta, and blue bars. The Y or luminance information is represented in this signal by the displacement of each pulse below the blanking level. The yellow bar has a comparative luminance value of .89 which is the greatest of the five color bars and is the result of adding the luminance of the red bar (.30) and that of the green bar (.59). The blue bar has the least value of luminance (.11) and the magenta luminance value of .41 results when the blue and red luminance values are combined.

With the generator set up as just indicated, the chroma switch was then thrown to the OFF position. This action removed the chrominance

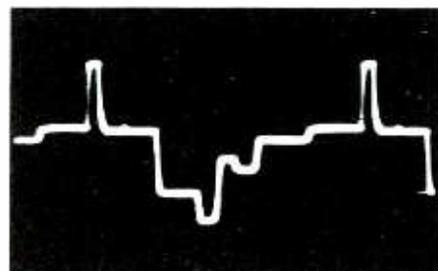


Fig. 3. Same Signal As in Fig. 2 Except That the Chroma Switch Is at the OFF Position. The Y Signal Remains.

information from the output signal. The waveform of Fig. 3 resulted and is an indication of the relative luminance levels just mentioned for the five color bars.

Fig. 4 is identical with Fig. 2 except that the video-polarity switch was thrown to the negative position for Fig. 4. This feature is useful in obtaining the correct polarity of signal when the video signal is introduced to different stages of a color receiver.

The waveform of Fig. 4 was further changed by throwing the Y

switch to the OFF position. This action removed the Y component from the signal and left the chrominance information only. The resultant waveform appears in Fig. 5.

When the function-selector switch is set at the Q and I position, the waveform of Fig. 6 is obtained; and when it is set at the R - Y and B - Y position, Fig. 7 is obtained. These figures appear to be exactly alike; however, there is a relative phase difference of 33 degrees between the 3.58-mc portions of the two signals, and this is sufficient to pro-

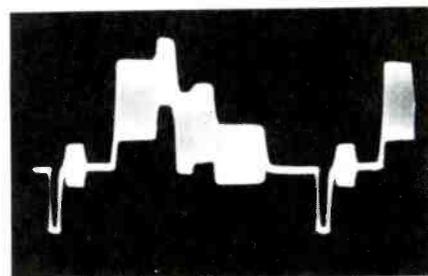


Fig. 4. Five-Color-Bar Signal of Fig. 2 But With the Video Polarity Switch Set at the Negative Position.

duce the required color differences. With the function-selector switch in either of these two positions, either or both of the two color-bar signals can be removed by throwing the I and R - Y control switch or the Q and B - Y switch.

Figs. 8 and 9 will serve to illustrate how the color-bar generator may be used to check and adjust the hue phase control and the quadrature transformer of a color receiver. The waveforms in these figures were ob-

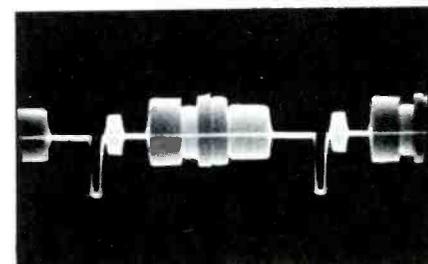


Fig. 5. Five-Color-Bar Signal of the Hickok 655XC With the Y Switch at the OFF Position. The Chrominance Signal Remains.

tained during the procedure described as follows: The RF output of the 655XC color-bar generator was connected to the antenna input terminals of a color receiver through a suitable matching network such as the Hickok 75, and the generator controls were set to provide an I and Q signal since this particular receiver was of that type. An oscilloscope was connected to a test point at the cathode of the Q-channel phase splitter. The operating controls of the color receiver were set as for normal operation

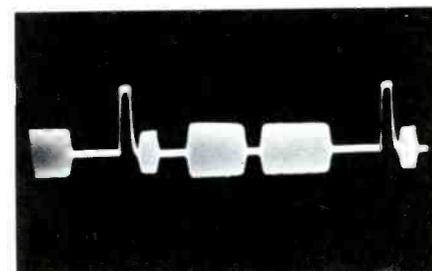


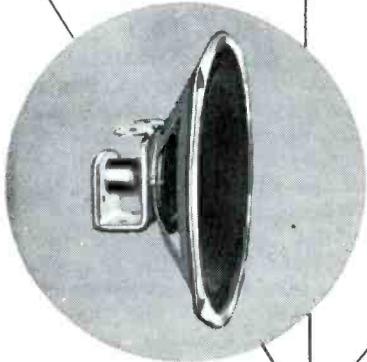
Fig. 6. The I and Q Signal Output From the Hickok 655XC.

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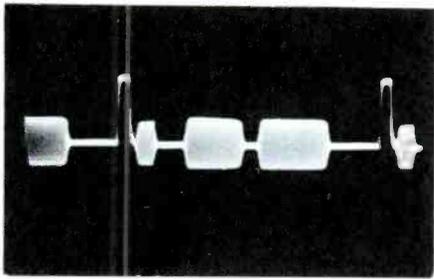


Fig. 7. The R-Y and B-Y Signal Output From the Hickok 655XC.

when viewing a color transmission. The generator supplies both I and Q signals; but with proper functioning of the receiver, only the Q-bar signal would be evident at the test point mentioned. The I bar would fall on the zero axis, as in Fig. 8. If the hue phase control were misadjusted, the I bar would fall above or below the axis, as shown in Fig. 9. Proper adjustment of the hue phase control would then cause the I-bar indication to move toward the axis and disappear there.

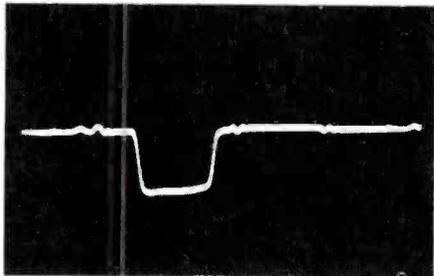


Fig. 8. Waveform Obtained at the Q Phase Splitter of a Color Receiver When I and Q Signal Output From the Hickok 655XC Is Applied to Receiver Input. The Waveform Indicates Correct Adjustment of the Hue Phase Control of the Receiver. A Signal of Negative Polarity Is Obtained at This Point.

After making the hue phase adjustment as indicated, the scope was moved to a corresponding point at the I-channel phase splitter to check for correct adjustment of the quadrature transformer. Correct quadrature adjustment would be indicated by an I-bar signal only, with the Q bar on the axis. Under these conditions, the I and Q channels would be demodulating the color subcarrier with a relative

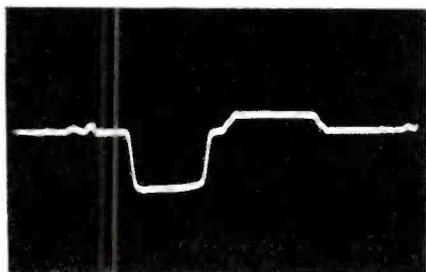


Fig. 9. Waveform Obtained As in Fig. 8 But With Incorrect Adjustment of the Hue Phase Control of the Receiver.

phase of 90 degrees or in quadrature with each other. If the Q bar were visible, the quadrature transformer should then be adjusted to make the bar disappear on the axis. When both bars are visible, there may be some question in the technician's mind as to which is the I or Q bar. This can be easily determined by throwing either the I or Q toggle switch and noting which bar disappears.

The foregoing adjustments are easily made with the aid of the oscilloscope and color-bar generator, and they take less time than it does to

describe them. Although the effect of such adjustments could be noticed on the screen of the color tube, innumerable combinations could occur; and it is highly improbable that the technician could ever arrive at the correct adjustment by observing the color screen alone. The use of the scope and the color-bar generator affords a positive indication.

Inasmuch as the Hickok 655XC color-bar generator also provides R - Y and B - Y signals, the same type of adjustments that have just been described could also be per-



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formed on a receiver which demodulates on the R - Y and B - Y axes.

Figs. 10 and 11 show the response of the I and Q channels, respectively, to the 5-color-bar signal. The oscilloscope was connected to the same test points previously mentioned. Starting from the left in each waveform, we see first on the zero axis a small disturbance which indicates the position of the horizontal sync pulse. This is followed by the relative step levels of the green, yellow, red, magenta, and blue bars in that order. It is interesting to note

that these levels and polarities correspond to the specified relative amplitudes and polarities for these colors, as recorded in Table I of Mr. Ennes's article "TV Colormath" in the June issue of the PF INDEX. (Allowance must be made for the fact that the Q-channel test point was located at a point of negative Q signal; and therefore, all the polarities of the Q-channel waveform must be reversed for proper interpretation.)

To quote from the table just mentioned, the relative amplitudes in the Q channel should be green -0.525,

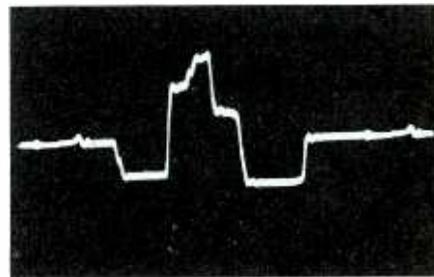


Fig. 10. Waveform Obtained at the Cathode of the I Phase Splitter When the Five-Color-Bar Signal Output From the Hickok 655XC Is Applied to the Receiver Input Terminals.

yellow -0.31, red +0.21, magenta +0.525, and blue +0.31. For the I channel, the relative amplitudes would be green -0.28, yellow +0.32, red +0.60, magenta +0.28, and blue -0.32.

If any marked deviation from these relative amplitudes or polarities is observed in the waveforms, some malfunction or misadjustment of the I or Q channel is indicated.

Another interesting feature to note in Figs. 10 and 11 is that the

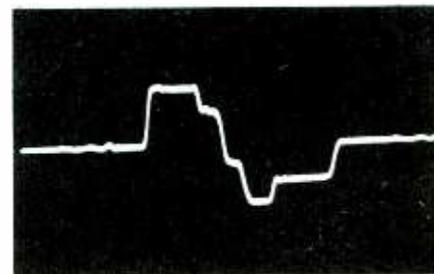


Fig. 11. Waveform Obtained at the Cathode of the Q Phase Splitter When the Five-Color-Bar Signal Output From the Hickok 655XC Is Applied to the Receiver Input Terminals.

square-wave response of the I channel appears to be better than that of the Q channel. This is to be expected since the I channel is designed for a bandpass of about 1.5 megacycles, whereas the Q channel is designed for a bandpass of only about 500 kc.

The preceding examples should give some indication of the usefulness and application of a test instrument such as the Hickok 655XC color-bar generator when servicing or adjusting color receivers.

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Shop Talk

(Continued from page 5)

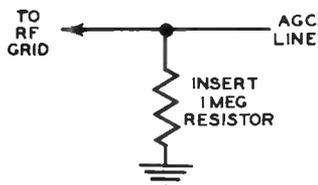
tuner. If this is so, insert a 470,000-ohm, half-watt resistor in the line before carrying out the foregoing test.

The RF Amplifier Tube

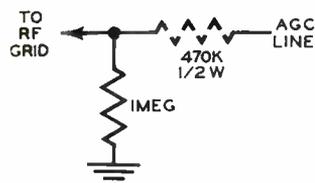
A second factor in the sensitivity of a television tuner is the RF amplifier tube. Improvement from this angle can be achieved in one of two ways — either by using another stronger tube of the same type or by substituting a tube with a different type number. The latter tube should have a higher mutual conductance but otherwise similar characteristics. Let us consider the first approach.

A. Choosing the Hottest Tube. In any group of similar tubes, measurements with a tube checker will reveal that some are hotter than others. The best test for this is with a transconductance (g_m) type of tube checker. When you find the tube with the highest g_m , use it in the RF stage of the tuner. The mere use of this tube, however, does not assure better performance because of the presence of interelectrode tube capacitance. This may vary enough from the capacitance of the original tube that the RF circuits will be detuned, and thereby any gain increase brought about by the rise in mutual conductance will be nullified. Hence, to obtain full benefit from a hot tube, the circuit should be carefully realigned. It is recognized that this procedure is not something which is carried out readily; moreover, in moderate and strong signal areas, any decrease in stage gain will frequently have no noticeable effect. But when you are fighting for every ounce of stage gain, the foregoing procedure will pay off.

The question of RF tuner alignment and how important it is will be



(A) IF-to-RF Isolation Already Provided.



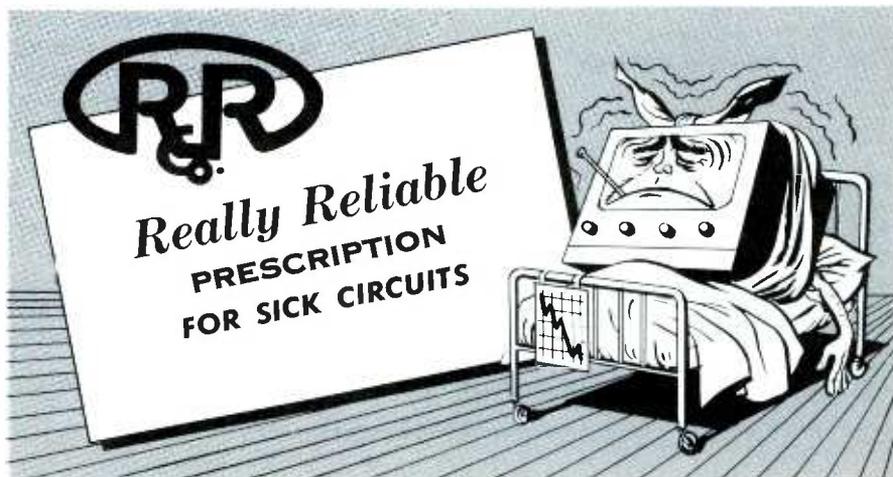
(B) A 470K-Ohm Resistor Inserted For IF-to-RF Isolation.

Fig. 2. Shunting the AGC Line to Ground With a 1-Megohm Resistor.

found, in the final analysis, to depend upon how much signal you have. In a strong signal area, there is considerable leeway available before the picture is noticeably affected. The RF response curve can be peaked, double-humped, or even skewed off to one side; yet to most observers no apparent change will be visible. (This test was made using trained service technicians who were carefully instructed to look for picture degradation, smearing, interference, and background noise.) The situation changes markedly, however, when the

signal level drops. It is toward the latter condition that this discussion is directed.

B. Substituting Other Tubes. Increased tuner gain can also be achieved by substituting other closely related tubes which inherently have a higher g_m . The 6AG5, 6BC5, and 6CB6 tubes offer an excellent illustration of this. With a plate voltage between 200 and 250 volts, the 6AG5 has a g_m value of 5,000 micromhos, the 6BC5 has a g_m value of 5,700



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micromhos, and the 6CB6 has a g_m value of 6,200 micromhos. Since amplifier gain is directly proportional to g_m , a stage using the 6CB6 will provide roughly 24 per cent more gain than the same stage using a 6AG5. This, then, is an excellent reason for using 6CB6's in place of 6AG5's. Precautions to observe in this exchange are: (1) that circuit realignment should also be carried out and (2) that the suppressor grid of the 6CB6 is not internally connected to the cathode as it is in the 6AG5. Hence, a check should be made to insure that the socket pin for the suppressor grid is properly connected when a 6CB6 is substituted for a 6AG5.

The B+ Voltage

The gain of an amplifier is also governed by the value of B+ plate and screen voltage used. In general, the higher the plate voltage, the greater the gain. In the 6AG5, for example, a g_m of 4,500 micromhos is obtained when the screen and plate voltages are both 100 volts. If we raise these to 125 volts each, the g_m value rises to 5,100 micromhos, or an increase

of about 14 per cent. However, it is interesting to note that further increase to 250 volts for the plate (and 150 volts for the screen) does not give any high g_m figure. As a matter of fact, there is a slight decrease to 5,000 micromhos. Therefore, the best voltage value to use would be 125 volts; anything beyond this is wasteful of power.

The source of much of the preceding data is any receiving-tube manual. This will tell you how much mutual conductance a certain value of plate voltage will produce. In addition, maximum ratings are also given, and these are important in making certain that the voltages you use do not cause the tube to exceed its dissipation wattage. Running a tube too hot will lead to shortened life and frequent replacement. The wattage being dissipated at the plate is computed by multiplying the voltage at the plate by the plate current. Screen dissipation is determined in a similar manner using screen-grid voltage and current.

If a change in grid bias is indicated when the plate voltage is raised, be sure to follow this recommendation. Most of the time, it simply means using another cathode resistor.

In very weak signal areas, boosters are often used ahead of the receiver. If this is the case, the proper procedure is to connect the booster to the set and observe the picture produced. After this if additional gain is still desired, the procedures discussed can be followed. A hot booster with a "souped-up" set can lead to sync-pulse compression or clipping or, worse still, to oscillations. With the use of cascode tuners and with the higher operating power of many stations, the need for boosters is not so pressing now as it was several years ago; however, boosters can still be useful in many situations.

REVIEW. The higher we go in frequency, the more important it becomes to arrange the various circuits in a receiver so that undesired interaction via stray fields is kept at an absolute minimum. Ordinarily, we might classify this as the engineer's problem and forget about it. However, service work frequently calls for parts replacement; and in high frequency circuits, altering lead dress or the placement of parts can have a noticeable deteriorating effect on receiver operation.

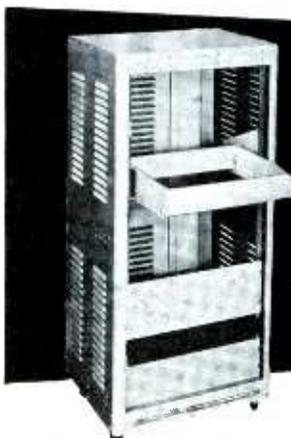
A companion subject to lead dress and circuit layout is shielding. While most of us know in a general way what shielding does, few of us really appreciate the underlying principles involved. Yet the theory (if we wish to call it that) is quite simple and excellently presented in an article that appeared in the June 1950 issue of "Wireless World." This is an English publication that is produced monthly by Iliffe & Sons, Ltd., Dorset House, Stamford Street, London, S.E. 1, England. Yearly subscription rates to Americans is \$4.50.

The article in question was entitled "Screening," which is the English equivalent of our "Shielding." The author is listed as "Cathode Ray" and is apparently a staff member who discusses some general topic each month.

There are two basic methods for preventing the field of one circuit from affecting any other circuit: either by diverting the course of the field or by cancelling it out with an opposing field. An illustration of the former method is given in Fig. 3. The magnetic lines of flux which the coil develops are kept within the coil enclosure by the high permeability of the container. The magnetic flux simply finds it easier to travel through the magnetic material than through air.

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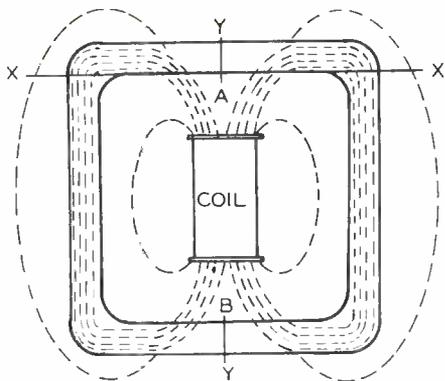


Fig. 3. Magnetic Shielding Afforded By a Metal Can of High-Permeability.

An electrical analogy to this magnetic behavior is shown in Fig. 4. The electromotive force of the battery E corresponds to the magnetomotive force of the current-carrying coil. The two high-valued resistances R1 and R2 correspond to the rather high magnetic reluctances of the air spaces at the ends of the coil. Before the low resistances of R3 and R4 are connected across the circuit, the full battery voltage appears across the ends of R1 and R2. When R3 and R4 are shunted across the circuit, their resistances are so low that the voltage difference between the ends of R1 and R2 is reduced to a very low value.

Let us now reconsider the coil in Fig. 3. When the high-permeability shield is placed over the coil, its low reluctance reduces to a very small value the magnetomotive force available for driving flux through the surrounding air. Consequently, there is very little flux in the air either immediately surrounding the coil or beyond the shield.

To carry the electrical analogy one step further, any break in R3 and R4 would remove their shunting effect and permit the full voltage of the battery to appear across the ends of R1 and R2. By the same token, any break or gap in the shield around the coil would permit some of the magnetic flux to escape and thereby nullify

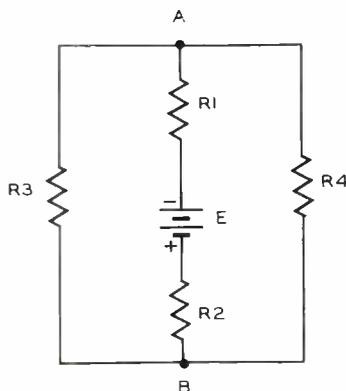


Fig. 4. Electrical Analogy of Fig. 3.

some of the shielding action of the can. The only place a gap is permissible is along such flux lines as YY in Fig. 3.

A high-permeability shield, such as one made of mumetal, will function admirably at the low frequencies. When the frequency increases, the permeability drops; and at the radio frequencies, a shield of this type is not of much help. The problem can be better met at high frequencies by using a copper shield. The permeability of copper is about the same as that of air, and so it cannot divert the flux. However, copper does function as a shorted secondary turn wherein the current set up in it produces a field which opposes the field of the coil.

If the copper shield were placed very close to the coil, much of the field of the coil would be nullified, reducing the inductance of the coil to a very low value. This would reduce its usefulness in the circuit. If the shield is made large and roomy, however, its effect on the coil is small; yet at the same time, it neutralizes practically all of the coil field reaching it by developing an opposing field of its own. The lower the resistance of the copper shield to current flow, the more effective the shielding action becomes.

It is interesting to note in connection with a copper shield that the direction of current flow differs considerably from the direction of the flux lines shown in Fig. 3. Current flows in a continuous ring parallel to the turns in the coil. Hence, a gap along line XX in Fig. 3 would be permissible; but one along YY perpendicular to the turns in the coil would interrupt the shield currents and render the shield useless.

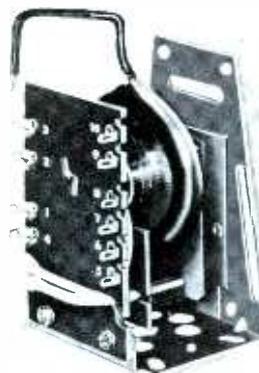
Electric Shielding

Thus far nothing has been said about grounding the shield; and indeed, so far as magnetic shields are concerned, grounds are of no particular consequence. A ground connection does become important in preventing electric (as distinguished from magnetic) fields from extending beyond their immediate area.

In Fig. 5A, V represents some component which has a large potential with respect to ground. The electric field is indicated by the dotted lines which indicate that every point in the surrounding space is under the influence of this electric field.

If we take a metal box and place it over V, the electric lines of force from V travel to the nearest surface of the metal box. See Fig. 5B. In

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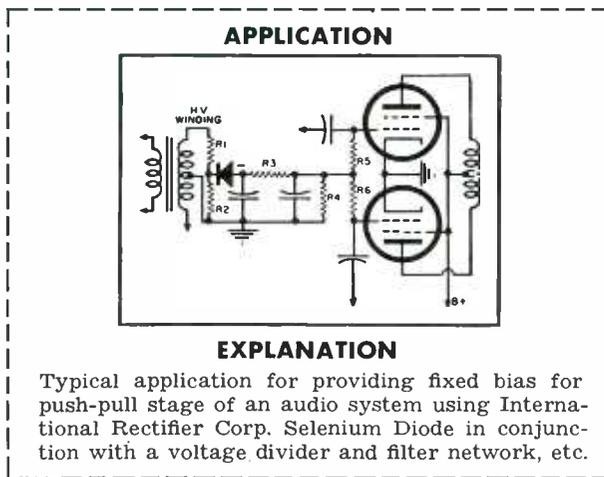
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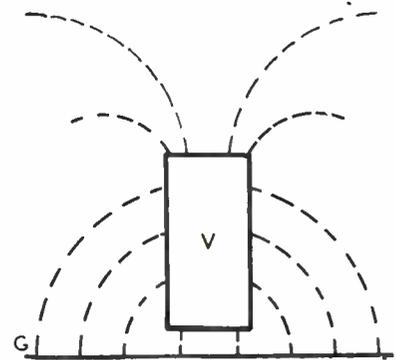
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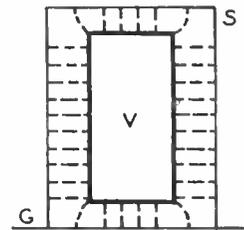
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this way, all the lines are returned to ground, and no portion of the field appears outside the metal box or shield.

For most effective shielding, the electrical resistance of the metal box should be quite low. For high



(A) Unshielded.



(B) Shielded by Metal Box or Screen of Low Resistance.

Fig. 5. An Electrical Field Produced by Potential V.

frequencies or where the shielding is critical, two shields may be used, one inside the other. It is also possible to achieve excellent shielding by using mesh screens instead of a completely enclosed surface. The lines of force will terminate on the screen wires, if they are grounded; and very little of the electric field will extend out between the wires. Straight, vertical screen wires are

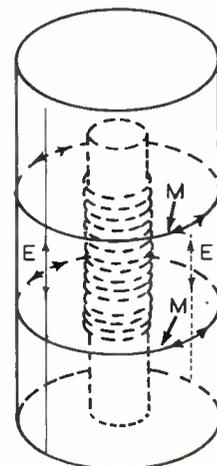


Fig. 6. An Electromagnetic Shield Showing Directions of Magnetically Induced Currents M and Electrically Induced Currents E.

best. A vertical spiral or coil of wire is not very effective because it would place a comparatively large resistance and inductance between the upper part of itself and ground.

As with magnetic screens, an electric shield should not be too close-fitting. Such a screen increases the capacitance to ground of whatever it is shielding; it also increases the currents flowing in the screen and raises the potential difference over the screen surface. Shielding is most effective when the over-all surface is all at ground potential.

Frequently, it is necessary to shield both the electric and magnetic fields of a component. For this we can use a grounded metal can which has a low resistance to current flow. See Fig. 6. The lines marked M indicate the current flow set up by the magnetic field, while the E-lines indicate typical current paths established by the electric fields. If the can must contain seams or joints, it is better to have them affect E than M.

If it is desired to stop electric (capacitive) coupling without interfering with magnetic coupling, say in

a transformer, then the proper approach is shown in Fig. 7. The shield between primary and secondary windings does not form a complete circular path; the insulating strip between the overlapping edges of a grounded, nonmagnetic metal sheet prevents any current flow due to magnetic lines of flux; and this, in turn, cannot establish a counteracting magnetic field. At the same time, the metal strip is grounded and effectively prevents electric fields from passing.

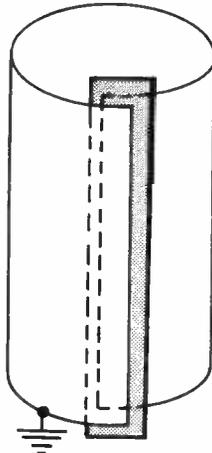


Fig. 7. Shield Which Allows Magnetic Coupling But Provides Electric Shielding.

If magnetic shielding is desired without affecting an electric field, it can be accomplished with a set of insulated rings parallel to the turns in the coil like hoops around a barrel.

In summary, the requirements for various types of shielding can be given as follows:

Magnetic shielding for DC or low-frequency AC requires the use of high-permeability metal which provides a continuous low-reluctance path for magnetic flux.

Magnetic shielding for high-frequency AC requires the use of high-resistance path for induced currents at right angles to the flux paths.

Electric shielding requires low-impedance conduction paths to ground and may be easily accomplished except at the highest frequencies.

Electromagnetic shielding requires a combination of both electric and magnetic shielding.

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Audio Facts (Continued from page 33)

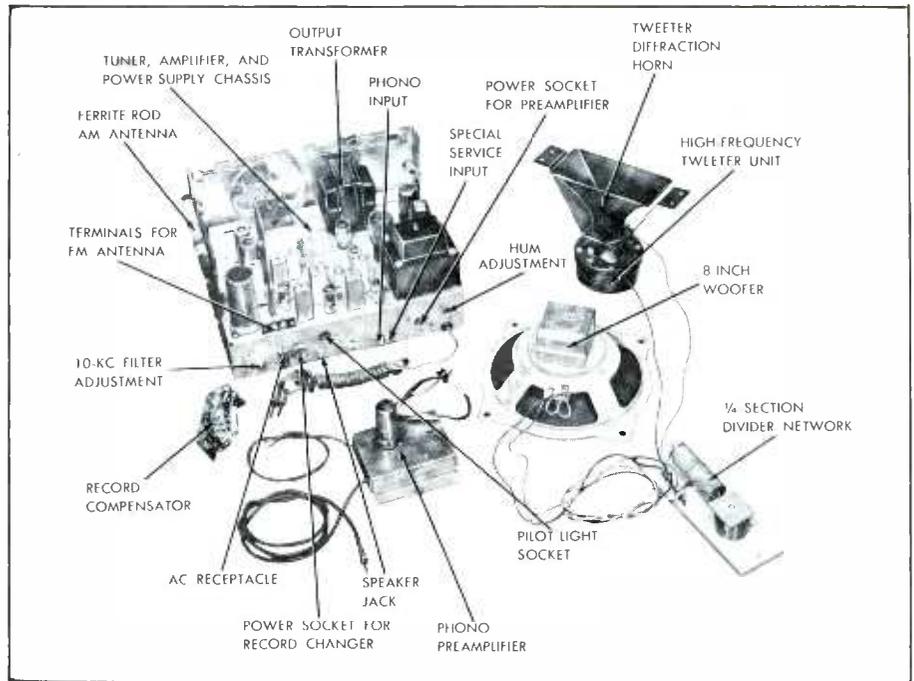


Fig. 2. View of Equipment Used in Capehart Model RP-154.

is a GE triple-play variable-reluctance cartridge. This separate preamplifier provides equalization by virtue of the feedback circuit around the second section of the 6SC7 tube and draws its power from the main chassis. The output cable connects to the phono input on the tuner amplifier chassis, and the input cable connects to the output of the record compensator.

The record compensator (Figs. 1, 2, and 4) is inserted between the pickup and preamplifier to equalize and compensate for the characteristics of the record being played. Its five positions are marked as follows:

Position No. 1	LP
Position No. 2	AES
Position No. 3	FLAT
Position No. 4	HC1
Position No. 5	HC2

Positions 1, 2, and 3 are self-explanatory; positions 4 and 5 provide

high-frequency roll-off in sufficient amounts to reduce the surface noise of records with poor or worn surfaces.

Enough flexibility of control is available in all modes of operation so that it should not be difficult to obtain satisfactory tonal balance.

All of the foregoing items are very important in a high-fidelity system, but the importance of the loudspeaker upon the results to be obtained from the system deserves special consideration. The loudspeaker performs the critical function of converting the electrical signal fed to it into an acoustical signal which can be recognized by the ear as being a faithful reproduction of the original sound.

A loudspeaker system composed of multiple units, a divider network, and a suitable enclosure is usually required if smooth, clean, and wide-range musical reproduction is to be

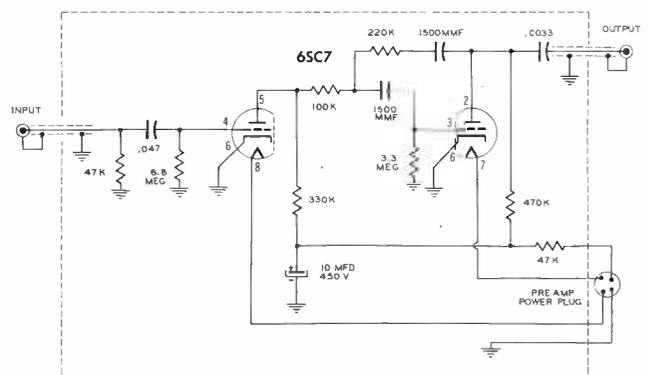


Fig. 3. Schematic of Phono Preamplifier.

enjoyed. This pattern has been followed in the Model RP-154, and the desired high quality of reproduction has been obtained because of the good design and careful selection of the components used — namely, the woofer, tweeter, divider network, and enclosure.

The 8-inch woofer, high-frequency tweeter, and the divider network are shown in Fig. 2. These mount in the left half of the cabinet which is enclosed on all sides. The cubic content of the resulting enclosure is sufficient for good matching with the 8-inch woofer. No sound-deadening material is used on the interior surfaces of the enclosure.

The high-frequency tweeter is an efficient smooth-operating unit which matches very well with the 8-inch woofer. The diffraction horn fitted to it distributes the high frequencies over a wide area; otherwise, they would be heard only in a narrow concentrated beam.

Frequency division and smooth response at the crossover point are provided by: (1) a simple quarter-section divider network (Figs. 2 and 5) employing a 4-mfd capacitor and a 0.47-mh coil, (2) the rather sharp

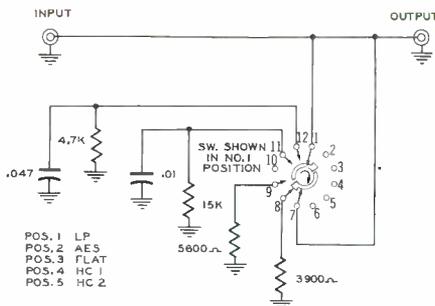


Fig. 4. Schematic of Record Compensator.

low-frequency cutoff of the horn-loaded tweeter, and (3) the high-frequency roll-off of the woofer.

The Model RP-154 was designed for use as a music system in the home.

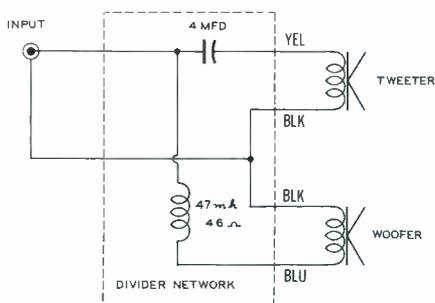


Fig. 5. Schematic of Loudspeaker System.

Consequently, best results are to be realized when listening is done under conditions similar to those found in the usual parlor or living room. The carpet, rugs, drapes, and upholstered furniture with which the room is furnished cut down on reverberation and are responsible for a deadening effect. The amount of brilliance or tonal balance suitable for such conditions would not be at all suitable in a "live" room possessing an empty-hall effect.

Most listening rooms in the home are not really large; and since comparative quiet usually reigns, very little audio power is needed to fill them. The reserve power of the Model RP-154 is more than sufficient to take care of the occasional peaks found in most musical selections.

The Capehart Model RP-154 is an interesting example of the present design trend to packaged, "all-in-one-cabinet" units for the high quality reproduction of music.

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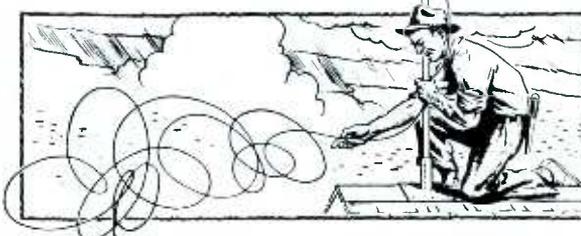
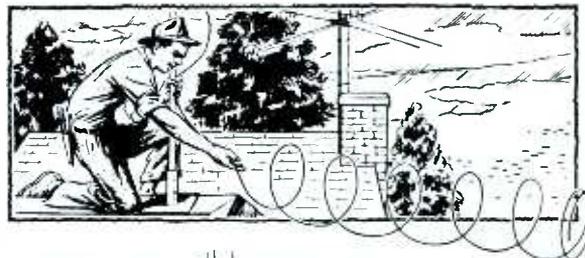
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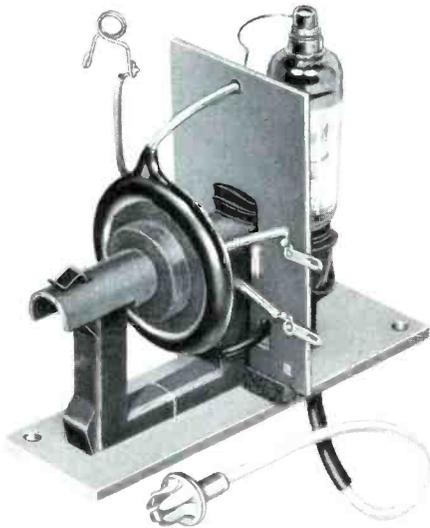
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(Continued from page 31)

shown as waveforms W1 and W2 in Fig. 8-26. For proper operation of the phase detector, it is necessary to change W2 into a saw-tooth waveform; and this is done by the integrating action of resistor R6 and capacitor C4. The resulting saw-tooth waveform is W3 in Fig. 8-26. Waveform W4 is this saw-tooth signal as it is applied to the phase detector by means of capacitor C3.

The action of the phase detector depends upon the simultaneous application of the aforementioned signals, but its operation can best be explained by considering the application of the signals separately. Let us start with the sync pulses as they are applied to

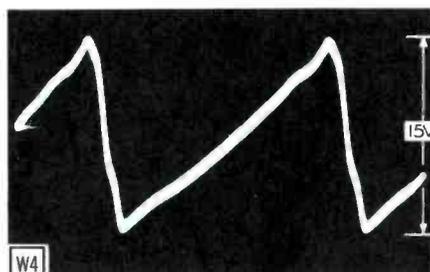
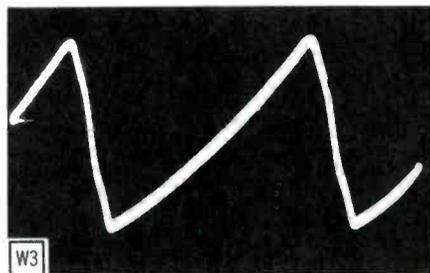
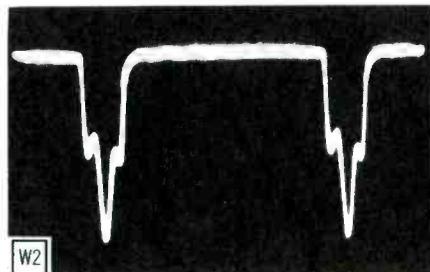
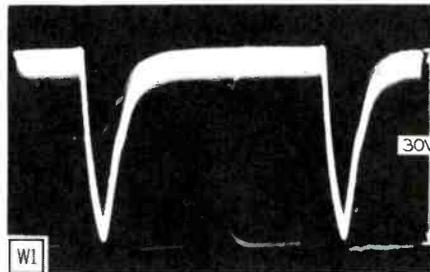


Fig. 8-26. Waveforms Applied to the Phase Detector.

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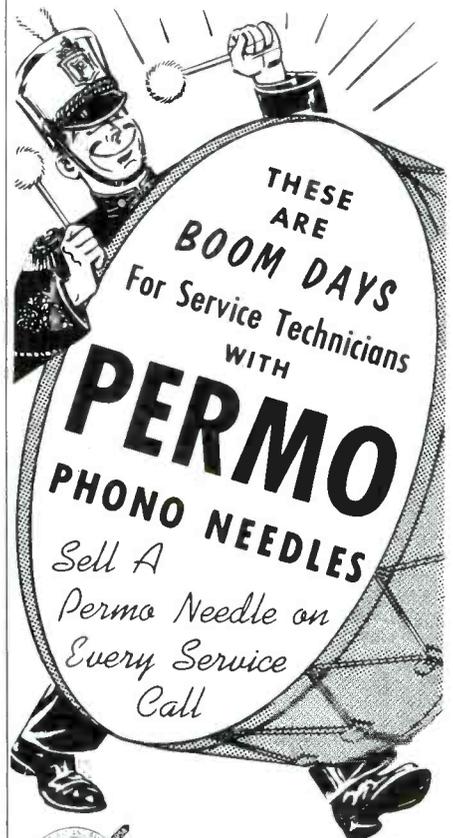
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the circuit of Fig. 8-27A which shows a redrawn version of the same phase-detector circuit that appears in Fig. 8-25.

The negative sync pulses applied to the diode cathodes have the same effect as positive pulses applied to the diode plates, and the pulses will cause current to flow in both diodes. During conduction, electrons flow out of the right side of C1 to the common cathode of the diodes where the electron flow divides between diode 1 and diode 2. If we first consider diode 1, the electrons flow from cathode to plate, through ground, and through the sync-amplifier tube to the left side of C1. In diode 2, the electrons flow from cathode to plate and into the top plate of the capacitor combination of C3 and C4. This displaces electrons from the lower plate of C4, and they flow through ground and through the sync amplifier to the left side of C1. Because of the excess of electrons on the left side of C1, this capacitor becomes charged in the polarity shown.

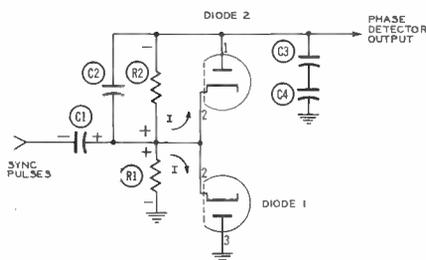
Between sync pulses, the diodes are not conducting and some of the charge on C1 leaks off through resistors R1 and R2. The electron flow during the discharge of C1 has two paths. Electrons flow from the left side of C1, through the power supply to ground, and from ground through resistor R1 to the right side of C1. This flow establishes across R1 a DC voltage which is approximately equal to the peak amplitude of the sync pulses. Electrons also flow from the left side of C1, through the power supply to ground, and from ground to the lower plate of the capacitor combination of C3 and C4. This displaces electrons from the top plate of this

capacitor combination, and the electrons move through R2 to the right side of C1. A DC voltage is developed across R2 in this manner. The voltages across resistors R1 and R2 are of equal values but opposite polarities, hence the voltage from the top of R2 to ground is zero. Since the top of R2 is also the output of the phase detector, no voltage is produced by the detector when the sync pulses are applied alone.

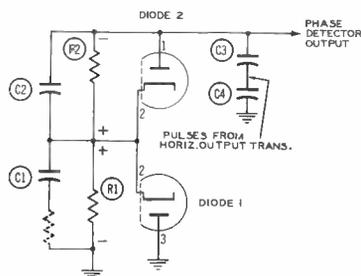
Let us consider the action of the phase detector when only the saw-tooth voltage is applied to the detector circuit. For this purpose, the circuit has been redrawn in Fig. 8-27B. The pulses from the horizontal-output circuit are applied to the junction of C3 and C4. Capacitor C4 integrates the pulses to form a saw-tooth waveform, and C3 couples this saw-tooth waveform to the plate of diode 2. Waveform W4 at this point has an amplitude of approximately 15 volts. The two diodes are connected in series to ground, thus a saw-tooth waveform of 7.5 volts appears across each of the diodes. To insure that these voltages are equal, the effective impedance of diode 2 is shunted by capacitor C2 in order to match the shunting effect of capacitor C1 on diode 1. In this way the impedances of the two circuits are made approximately equal, and hence the proper voltage division occurs when the saw-tooth signal is applied.

Due to the fact that the two diodes are connected back to back, diode 2 conducts on the positive half-cycle of the saw-tooth voltage and diode 1 conducts on the negative half-cycle. Each diode conducts while the other one is nonconductive. Conduction in diode 1 will develop a voltage across R1, and conduction in diode 2 will develop a voltage across R2. The polarities of these voltages are indicated in Fig. 8-27B. As with the sync pulses, these voltages are equal but of opposite polarities, and the detector produces no voltage in the output.

At this point, the reader may understandably ask, "If the sync pulses do not produce an output from the phase detector and if the saw-tooth feedback voltage does not produce an output, how can any control voltage be developed?" The answer to this question lies in the fact that when the two different signals are both applied to the detector circuit the instantaneous value of the saw-tooth voltage at the time of sync-pulse application acts to unbalance the total voltages across the two diodes in such a way that the DC voltages across R1 and R2 are also unbalanced. This unbalanced condition creates the control voltage.

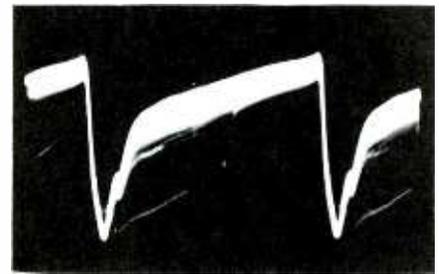


(A) With Sync Pulses Applied Alone.

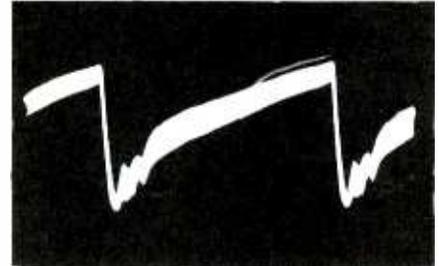


(B) With Saw-Tooth Voltage Applied Alone.

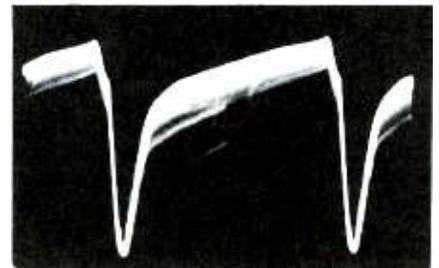
Fig. 8-27. Phase-Detector Action.



(A) Horizontal Oscillator Operating at Sync-Pulse Frequency.



(B) Horizontal Oscillator Too Slow.



(C) Horizontal Oscillator Too Fast.

Fig. 8-28. Waveform W5 Under Various Operating Conditions.

The observation of the waveforms representing the combined sync-pulse and saw-tooth signals across each diode is hampered by the fact that both the cathode and the plate of diode 2 are above ground potential. Both electrodes have a high impedance to ground; and when the ground lead of the scope is connected to the cathode, a considerable amount of hum is injected into the phase-detector circuit.

For this reason, in Fig. 8-28 we can show only waveform W5 which is the voltage on the cathode of diode 1 with respect to the plate of diode 1. The reader should use his imagination to visualize the plate voltage with respect to the cathode on this diode. The easiest way to do this is to think of a downward excursion of the waveform as being a positive voltage on the plate and an upward excursion as being a negative voltage.

It was stated previously that the charge on C1 between sync pulses was about 30 volts. An inspection of the circuit should reveal that this voltage is of such polarity that the diodes are biased in the nonconductive direction. This charge diminishes as C1 discharges; and by the time the next sync pulse arrives, the charge is just low enough to allow the diodes to con-

duct on the peaks of the pulses. This action is necessary to insure that only that portion of the saw-tooth waveform which occurs during the sync pulse has any effect on the output of the phase detector. The sync pulse applied to a circuit of this type should always have an amplitude about twice that of the saw-tooth waveform.

To explain the action of the phase detector when both signals are applied, we shall first assume that the sync pulses and the saw-tooth voltage are in phase. The waveform W5 which occurs in this case is shown in part A of Fig. 8-28. The sync pulse appears at the time when the retrace portion of the saw-tooth waveform is passing through the AC axis; this is a point of zero voltage for the saw-tooth waveform. The saw-tooth voltage neither adds nor subtracts from the sync-pulse voltage, and the diodes have equal applied voltages. Both diodes will conduct equally, and no DC voltage can appear in the output of the phase detector.

The sweep oscillator in the receiver can run either faster or slower than the frequency of the sync pulses. If it were to run slower, the sync pulses would arrive at the phase de-

tor before the saw-tooth waveform crossed the AC axis. The sync pulse would appear on the positive portion of the saw-tooth voltage across diode 2, and the two voltages would add. The sync pulse would appear on the negative portion of the saw-tooth voltage across diode 1, and the two voltages would subtract. Waveform W5 in part B of Fig. 8-28 shows the reduced voltage across diode 1 under this condition. The missing waveform across diode 2 would have a higher amplitude. Since diode 2 has the most applied voltage, it would conduct more than diode 1 and produce a higher voltage across its load resistor. This voltage is negative, and so the detector output voltage is also negative. This is the AFC or control voltage, and it is applied to the grid of the reactance tube which then alters the oscillator frequency to conform with that of the sync pulses.

If the oscillator tends to run faster than the frequency of the sync pulses, the sync pulses would appear at the phase detector after the saw-tooth waveform crossed its AC axis. Now the sync pulses would be superimposed on the negative portion of the saw-tooth voltage across diode 2, and the voltages would subtract. Across

diode 1, meanwhile, the sync pulse would appear on the positive portion of the saw-tooth voltage, and the two voltages would add. Waveform W5 in Fig. 8-28C shows the increased voltage across diode 1 under this condition. The missing waveform across diode 2 would have a lower amplitude. Diode 1 will therefore conduct more current than diode 2, and a positive voltage will be produced at the output of the phase detector. A positive voltage applied to the grid of the reactance tube will return the oscillator to the correct frequency.

It should now be evident that frequency correction takes place from either direction. If the oscillator tends to run slow, a negative voltage which speeds up the oscillator is produced. If the oscillator tends to run fast, a positive voltage which slows down the oscillator is produced.

The output voltage from the phase detector is passed through a filter circuit before it is applied to the reactance tube. This filter is designed to remove any fluctuations in the control voltage and, especially, to minimize the effects of random noise pulses which could affect the stability of the horizontal oscillator.



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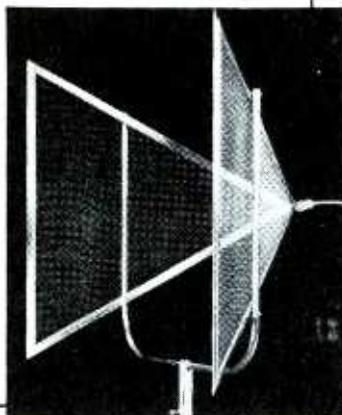
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Reactance Tube

The basic principle of operation for the vacuum tube is that the control grid voltage can control the plate current in the tube. If a constant plate voltage is applied to a tube and the grid voltage is varied, the tube will appear as a variable resistance to any circuit connected to the plate. This is the basis for the operation of the capacitive reactance tube V2 in the schematic of Fig. 8-25. Capacitor C8 is connected from the top of the oscillator tank coil, in series with V5 and R8, to the bottom of the tank coil. When the grid bias of V2 is varied by the phase-detector output voltage, the plate resistance of V2 is varied. Since this plate resistance is in series with C8, the effective capacity which C8 contributes to the oscillator tank circuit is also varied. In this way the oscillator frequency is varied.

If the control voltage on the grid of the reactance tube goes in a positive direction, the plate resistance offered by the tube decreases and C8 introduces more capacitance into the oscillator tank circuit. This action tends to lower the frequency of the oscillator. On the other hand, if the control voltage goes in a negative direction, the plate resistance of the tube increases. There is less capacitance shunted across the tank circuit and the oscillator frequency increases.

Resistor R9 is a voltage dropping resistor which reduces the amount of plate current drawn by V2. Resistors R7 and R8 are so proportioned that a portion of the oscillator cathode voltage is applied to the reactance-tube cathode as an initial fixed bias. If the grid of the reactance tube were not biased negatively, a positive control voltage would cause a detrimental flow of grid current in the reactance tube. In addition, the fixed bias establishes the control-grid voltage at a position on the tube curve where the control exerted by the grid is linear. This insures that equal increments of change in the control voltage produce correspondingly equal changes in plate current.

Oscillator

The horizontal oscillator V3 in the schematic of Fig. 8-25 is connected in a modified Hartley circuit and operates as a class-C, sine-wave oscillator. Grid bias for the oscillator is derived by grid rectification of the positive portions of the sine-wave voltage developed across the tank coil L1. Capacitor C10 receives a charge when grid current flows on each positive peak and discharges through resistor R10 to hold the grid

below the cutoff level for about 70 per cent of the cycle. Waveform W6A in Fig. 8-29 shows the voltage at the grid of the oscillator tube. It can be seen that the negative portion of this waveform is a sine wave but that the positive portion has been distorted. This distortion is a result of the signal developed at the point indicated for W7 in Fig. 8-25. In some circuits this point is grounded, and the waveform on the grid of the oscillator more closely approaches a sine wave as indicated by waveform W6B in Fig. 8-29. In this type of circuit a different means is employed for biasing the reactance tube since R7, R8, and C7 are eliminated.

Waveform W7 in Fig. 8-29 represents the output of the oscillator. The addition of waveforms W7 and W6B results in waveform W6A. The important feature of the output waveform is the fairly sharp positive peak, which incidentally causes the distortion in the positive portion of waveform W6A. This peak is required in order to drive the discharge tube properly.

Discharge Tube

The discharge tube V4 in the schematic of Fig. 8-25 operates as a conventional discharge stage such as has been described previously in this series. The stage is driven by wave-

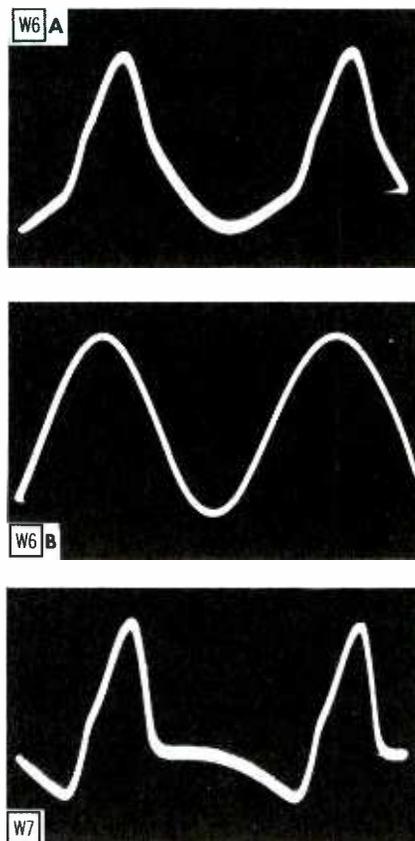


Fig. 8-29. Oscillator Waveforms.

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form W8, shown in Fig. 8-30. Grid current flows during the positive peaks as shown by the flattened tops. Capacitor C11 obtains a charge during grid-current flow, and the discharge of this capacitor through resistor R11 holds the grid below cutoff except during the positive peaks. Thus, the tube acts as a switch by conducting during the positive peaks and by not conducting between these peaks.

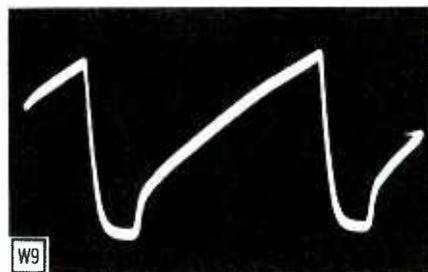
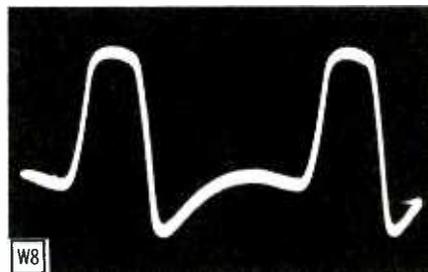


Fig. 8-30. Waveforms in the Discharge-Tube Circuit.

The saw-tooth waveform W9 in Fig. 8-30 is produced at the plate of the discharge tube. Proper shaping is achieved through the use of C12 and R13. The capacitor charges through resistor R12 while the discharge tube is not conducting and discharges rapidly through the tube when it is conducting. The trace portion of the saw-tooth waveform is formed by the charge cycle, and the retrace portion is formed by the discharge cycle. Resistor R13 is included to develop the trapezoidal waveform which is required for proper operation of the horizontal-output stage.

The Gruen circuit and many modifications of it have been used by several television manufacturers. These circuit modifications will, in many cases, cause the waveforms to be somewhat different from those shown here, and liberal interpretation will be needed in order to compare the various waveforms. The end product should always be some form of saw-tooth waveform which is applied to the horizontal-output stage.

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Tubes for Series Strings

(Continued from page 21)

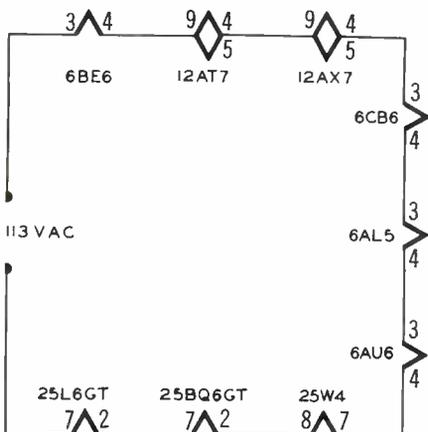
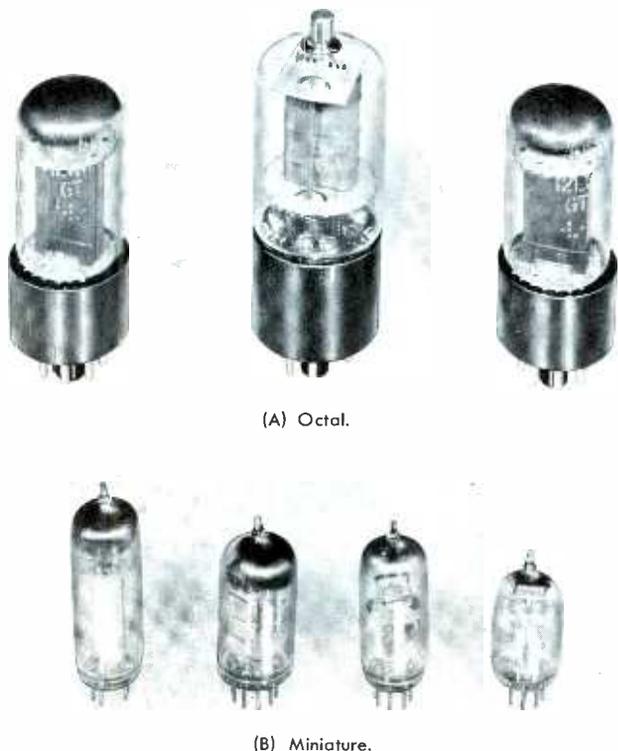


Fig. 2. Series-Filament String Composed of 300-Milliamper Tubes.

Notice particularly the power dissipation across V1 as compared to that across V2. Assume that the warm-up time for V1 is less than that for V2. Fig. 1B shows the electrical circuit values at the time when V1 completes its warm-up time and assumes its hot-resistance value of 21 ohms. V2 is still warming up; its resistance may be only 10 ohms. A marked surge of voltage appears across the filament of V1. When V2 attains its hot resistance, as in Fig. 1C, the voltages across the tubes equalize.



(A) Octal.

(B) Miniature.

TABLE I

RESULTS FROM TEST OF 300-MILLIAMPERE STRING IN FIG. 2.

Tubes	Max. Surge (volts)	Steady-State (volts)	Time Taken to Reach Steady State (seconds)
6BE6	10.0	6.8	43
12AT7	7.0	6.2	45
12AX7	22.0	6.1	21.5
6CB6	6.4	6.4	40
6AL5	13.5	6.1	35
6AU6	8.4	6.4	56
25W4	25.5	25.5	16
25BQ6GT	21.5	21.5	59
25L6GT	34.0	28.0	52.5

Further complications are imposed when the number of tubes in a series string is increased. When several tubes are slow in reaching the full value of their hot resistance, the voltage drops across these tubes are lower than their rated values. This leaves an excess of voltage to be distributed across the remaining tubes. Surge voltages are increased still further by the additional number of tubes.

Since the heater temperature determines the heater resistance at various times during warm-up time, it is apparent that if all tubes warmed up at the same rate and if the initial resistances were in the same ratio as the final resistances, the distribution of resistance in the series string would be the same at all times. Voltage surges would be minimized under these conditions.

Fig. 3. New 600-Milliamper Tubes. (Samples Courtesy of the General Electric Company.)

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TABLE II
GENERAL ELECTRIC
600-MILLIAMPERE FILAMENT TUBES

Tube Type	Heater Rating (volts)	Heater Rating (amps.)	Equiv. Type
3AL5	3.15	0.6	6AL5
3AU6	3.15	0.6	6AU6
3BC5	3.15	0.6	6BC5
3BE6	3.15	0.6	6BE6
3BN6	3.15	0.6	6BN6
3BY6	3.15	0.6	6BY6
3CB6	3.15	0.6	6CB6
5AQ5	4.7	0.6	6AQ5
5EK7A	4.7	0.6	6BK7A
5J6	4.7	0.6	6J6
5T8	4.7	0.6	6T8
5U8	4.7	0.6	6U8
5V6GT	4.7	0.6	6V6GT
12FK5	12.6	0.6	6BK5
12BQ6GA	12.6	0.6	6BQ6GA
12L6GT	12.6	0.6	25L6GT
12W6GT	12.6	0.6	6W6GT

To demonstrate surges in an actual string, nine tubes with 300-milliamperere filament ratings were selected at random and connected in a series-string arrangement. Since the drops in voltage across the combined tubes totaled 113 volts, this value of AC voltage was impressed across the string. A vacuum-tube voltmeter was used to record the largest voltage surge and also to record the final steady-state voltage across each filament. The time

necessary for the voltage to level off and reach a steady value was recorded with a stop watch. Fig. 2 shows a diagram of the tubes used and how they were connected in the string. Table I shows the largest voltage surges and the steady-state voltages across the filaments. The time taken for the tube voltages to reach a steady state is also recorded.

An examination of the figures given in Table I shows that three out of the nine tubes had extremely high surges of voltage. The 12AX7, which was connected for 6.3-volt operation at 300 milliamperes, was the worst offender with a surge of 22 volts; next was the 6AL5 with 13.5 volts; and the 25L6 had 34 volts across a filament rated at 25 volts. It should be noted that the steady-state voltages were unevenly distributed among the tubes. For instance, the 25L6 had a 28-volt drop and the 25BQ6 had only 21.5 volts across it. This can be attributed to a variation in hot resistance between the tubes. In most cases, this variation is small because it is one of the features over which the manufacturer has established a control limit. Normally, even though tubes are of different types, their hot resistance will be the same as long as their filaments have equal voltage and

TABLE III
RCA 600-MILLIAMPERE
FILAMENT TUBES

Tube Type	Heater Rating (volts)	Heater Rating (amps.)	Equiv. Type
3BC5	3.15	0.6	6BC5
3CB6	3.15	0.6	6CB6
5AN8	4.7	0.6	6AN8
5AT8	4.7	0.6	6AT8
5J6	4.7	0.6	6J6
5U8	4.7	0.6	6U8
12L6GT	12.6	0.6	25L6GT

current ratings. The surges in the circuit of Fig. 2 are probably greater than will be encountered in actual circuits, because no effort was made here to arrange these tubes for best results. The test was conducted only to illustrate how acute this problem can be.

Set manufacturers have tried numerous methods of tube arrangements in an effort to eliminate these voltage surges during warm-up time. Current-limiting resistors such as the Globar type are used, and in some cases the tubes are specially selected to meet the specific requirements. With all the precautions that are taken, surges sufficient to reduce tube life materially are still encountered in



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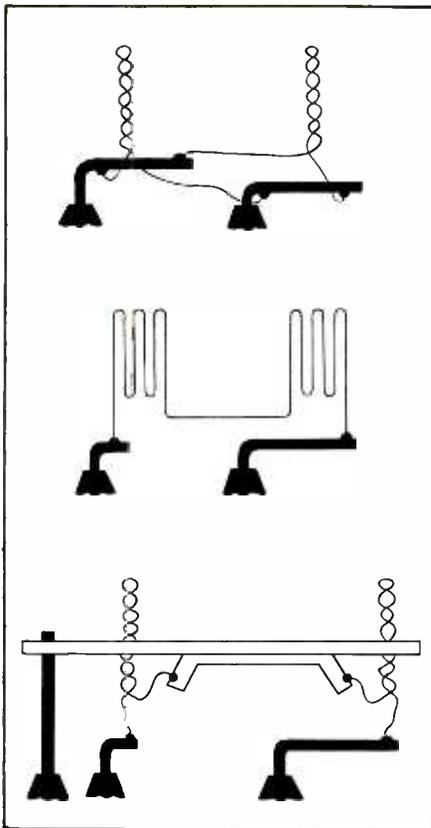


Fig. 4. Various Types of Heater Construction.

many of the series-string circuits that are in use in television sets today.

New 600-Milliamperre Tubes

As a solution to this trouble, some of the tube manufacturers have announced a new line of tubes especially designed for series-string operation in television receivers. The General Electric Company, for example, will produce the tubes that are shown in Table II. This table also shows the heater ratings and the equivalent tube types. Photographs of some of these tubes are shown in Fig. 3. RCA has also announced the release of seven tube types of 600-milliamperre heater operation. These types are listed in Table III. Note that the new filament-voltage ratings are indicated by the first figure in the tube-type number. With the exception of heater voltage and current ratings, electrical characteristics will remain the same as for the listed equivalent types.

We have stated that if all the tubes in a series string took the same length of time to warm up and if the initial resistances were the same ratio as the final resistances, the resistance distribution in the string would be the same and no surges could exist. This is, in effect, the approach that has been used in designing the new 600-milliamperre line of tubes.

The metal, the type of coating, and the structural shape of the heater are important factors in determining the length of time for warming up. In the past, several structural designs have been used in the construction of filaments. Some of these are drawn in Fig. 4. In the new 600-milliamperre tubes, the manufacturers have controlled the aforementioned factors to produce heaters with uniform warm-up periods. At the same time, they have maintained the cold resistances of all the new tubes in the same ratio as the hot resistances of the tubes. For example, the hot resistances of a 3AL5 and a 12BK5 are 5.25 ohms and 21 ohms, respectively. If the cold resistance of the 3AL5 is 2.5 ohms, then the cold resistance of the 12BK5 is:

$$R = \frac{21}{5.25} \times 2.5 = 10 \text{ ohms.}$$

In the past there have not been enough tubes with equal heater-current ratings to provide a complete line of tubes for a television receiver. This meant that set manufacturers had to use 300- and 600-milliamperre heaters connected in a series-parallel arrangement. Such an arrangement increased the difficulty of maintaining constant voltage drops across every tube. A complete line of the new 600-milliamperre tubes will make it possible to have a television set with one string of tubes (picture tube included). Total voltage drop across all tubes will probably be about 95 to 100 volts.

We should remember that the heater warm-up time will not necessarily be the time it takes for the tube to go into operation since that will be dependent upon the cathode used, its thickness, coating, and other factors. A heavier wire is used for 600-milliamperre heaters, giving them the additional advantage of sturdier construction. The new tubes are less likely to be affected by shock and vibration.

To see how these new tubes react in comparison with the 300-

TABLE IV
RESULTS FROM TEST OF
600-MILLIAMPERRE FILAMENT
STRING IN FIG. 5

Tubes	Max. Surge (volts)	Steady-State (volts)	Time Taken to Reach Steady State (seconds)
3FE6	3.8	3.1	9
5T8	6.0	4.6	9
5T8	6.4	4.6	8
3CB6	4.0	3.2	10
3AL5	4.0	3.1	9
3AU6	3.8	3.1	10
12W6GT	12.7	12.7	11
12BQ6GA	12.6	12.6	11
12L6GT	12.7	12.7	10

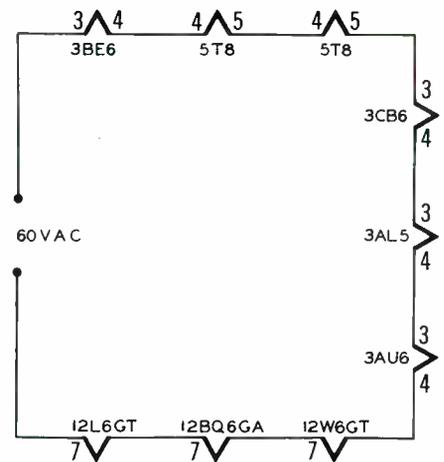


Fig. 5. Series-Filament String Composed of New 600-Milliamperre Tubes.

milliamperre tubes, surge-voltage readings were taken in a nine-tube string composed of one 3BE6, two 5T8's, one 3CB6, one 3AL5, one 3AU6, one 12W6GT, one 12BQ6GA, and one 12L6GT. Fig. 5 shows how these tubes were connected. The voltage readings and times are listed in Table IV. Compare this table with Table I. Although there were some slight voltage surges in the new tubes, the figures clearly indicate an improvement over the older types of tubes.

The advantages of series filaments in a television receiver are many. The transformer can be eliminated; and this means a reduction in size and weight of the chassis, a reduction in the spacing requirements of the picture tube because of the removal of magnetic fields, and a reduction in the power consumed in transformer losses. With less power dissipated, the set will operate cooler; and a cooler operating temperature will tend to reduce the failure of component parts. All of these are factors which lower the initial cost of the television receiver a matter of extreme importance to the set manufacturer.

When we consider these advantages, it is easy to predict that in all probability a large percentage of the forthcoming sets will be using these 600-milliamperre tubes for series-connected filament strings. To the service technician, this will mean that he will have to stock a larger selection of tubes. Probably he will have to modify his tube tester in order to handle tests on the new tubes with their different voltage and current ratings. On the other hand, it will mean that better sets can be sold for less money. With more sets in use, the service technician will benefit by increased business.

JAMES M. FOY

PF INDEX REPORTER

INDEX TO ADVERTISERS
September, 1954

Advertisers	Page No.
All Channel Antenna Corp.	56
Alliance Mfg. Co.	50
American Phenolic Corp.	60
American Screen Products	90
Arco Electronics, Inc.	74
Blonder-Tongue Laboratories Inc. ...	48
Bud Radio, Inc.	82
Bussmann Mfg. Co.	8
CBS Hytron	6, 24
Centralab Div. Globe-Union, Inc. ...	28 & 29
Chicago Standard Transformer Corp. .	18
Clarostat Mfg. Co., Inc.	32
Clear Beam Antenna Corp.	46
Cornell-Dubilier Electric Corp.	79
Eby Sales Co.	88
Electro Products Labs., Inc.	94
Electrovoice, Inc.	93
Electronic Instrument Co., Inc. (EICO).	61
Federal Telephone & Radio Co.	22
Fenton Co.	94
General Cement Mfg. Co.	38
Haldorson Trans. Co.	88
Hickok Electrical Instrument Co.	30
Hycon Mfg. Co.	64
International Rectifier Corp.	84
International Resistance Co. ...	2nd Cover
Jackson Electrical Instrument Co. ...	68
Jensen Industries, Inc.	40
Jensen Mfg. Co.	62
JFD Mfg. Co.	14
Jerrold Electronics Corp.	58
Littelfuse, Inc.	4th Cover
Mallory & Co., Inc., P. R.	10
National Electric Products	42
Ohmite Mfg. Co.	70
Oxford Electric Corp.	90
Perma-Power Co.	92
Permo Inc.	88
Planet Mfg. Corp.	85
Precision Apparatus Co., Inc.	26
Quam-Nichols Co.	78
Quietrole Co.	94
Radelco Mfg. Co.	52
Radiart Corp.	34 & 35
Radio Corp. of America	83 & 92
Radio Electronics	87
Radio Receptor Co., Inc.	81
Raytheon Mfg. Co.	12
Regency Div., I.D.E.A., Inc.	1
Sams & Co. Inc., Howard W. ...	98, 128
Shure Bros., Inc.	69
Sonotone Corp.	72
South River Metal Products Co.	54
Sprague Products Co.	2
Suprex Electrical Instrument Co. ...	86
Sylvania Electric Products Inc. ...	16 & 17
Technical Appliance Corp.	20
Triad Transformer Corp.	91
Triplett Electrical Instr. Co. ...	3rd Cover
United Catalog Publishers, Inc.	84
University Loudspeakers, Inc.	66
V-M Corporation	71
Walsco Electronics Corp.	36
Ward Products Corp.	4
Webster Electric Co.	76
Weller Electric Corp.	80
Weston Electrical Instr. Corp. ...	44 & 45
Wright Steel & Wire Co., G. F.	87
Xcelite, Inc.	85



As was generally expected, color television did not become a major, direct factor in the service field immediately after the adoption of the NTSC standards by the FCC.

The development, production, and sale of color television receivers to date have not been great enough to account for any percentage of servicing. The percentage of service technicians which has been called upon to service color television receivers is close to zero. There is little doubt, however, that this situation will exist for too long.

Several factors can account for the seemingly slow pace of color television up to the present time. One of the factors has been, of course, the number of color programs available, or rather the lack of them. Network color schedules should show a considerable increase this fall and will undoubtedly continue to expand. In addition to network telecasts in color, many local programs will also be available in color. As color programming increases, so will the interest of the consumer or prospective purchaser of color television receivers.

Another major factor has been the unavailability of any quantity of color television receivers in what is termed large-screen size at prices that will be attractive to the general public. The stumbling block here has been the design, development, and manufacture of large-screen, color picture tubes that do not require a great deal of complicated circuitry. The solution to this is a necessity before color television receivers will be mass produced and sold.

Large-screen, color picture tubes have been announced, are in production, and will soon be available. Then there will undoubtedly be gradual development toward mass production, lower costs, and an increasingly greater number of people who will purchase color television receivers. As the percentage of people who own color receivers increases, so will the percentage of the service technician business be increased from the servicing of these receivers.

It will be quite some time before color receiver servicing will detract from the present or prospective amount of servicing of monochrome TV receivers, radios, audios, etc., and therefore it must be considered as an addition to present servicing business. If this color receiver servicing is to be a part of your business, then it must be included in your plans for the future.

Color television servicing is not simple. To adjust and service color television receivers, the technician will require knowledge of new terms, new circuits, and new methods. He should obtain this knowledge through study prior to the time that it becomes a factor or a part of his every-day business. This study will require time and investment.

We have tried in the planning and development of the "Color TV Training Series" to first give the basic fundamentals of colorimetry, color television transmission standards, and signal make-up that must be known and understood prior to delving into receiver circuits.

Circuit description, analysis, and servicing procedures will then be given from actual examination and experience obtained in the adjusting and servicing of production color television receivers.

We hope that this series becomes a part of your present planning and that it will assist you in making your future color television receiver servicing more pleasant and, above all, profitable.

L.H.N.

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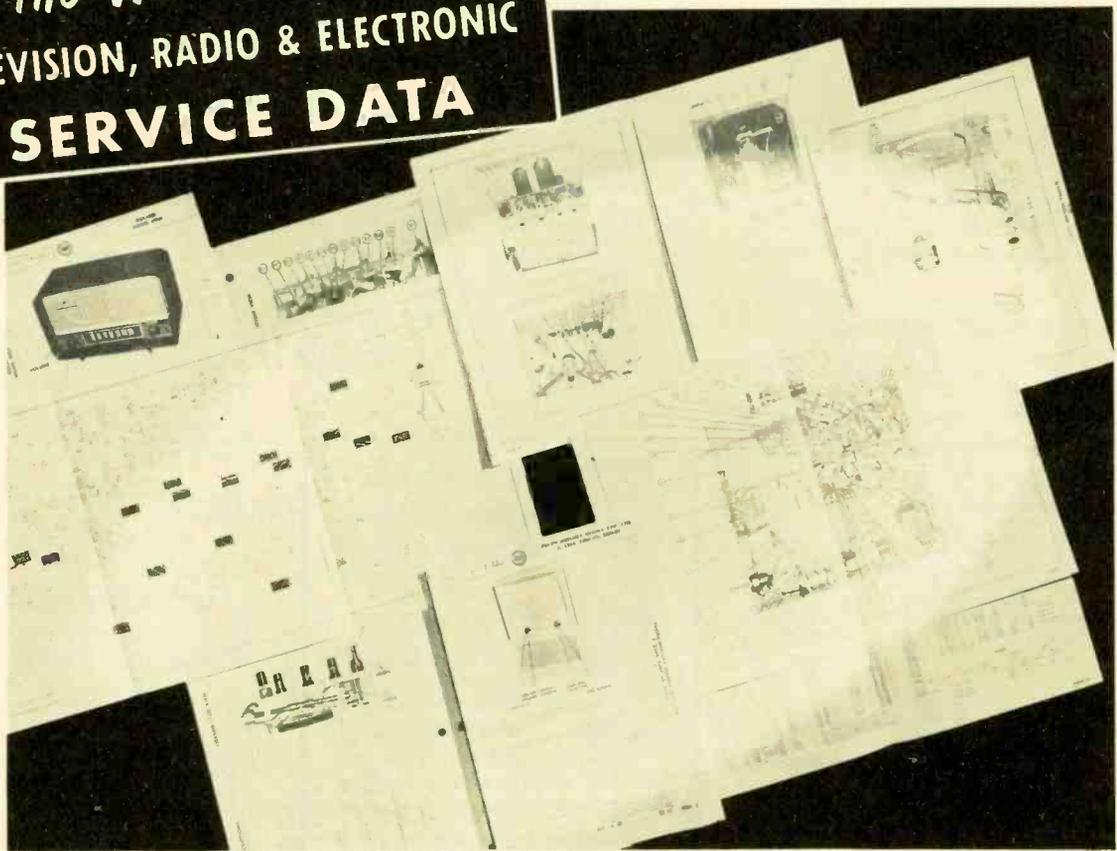
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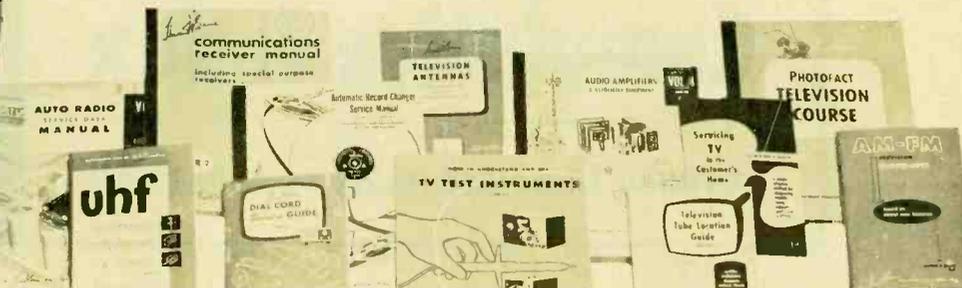
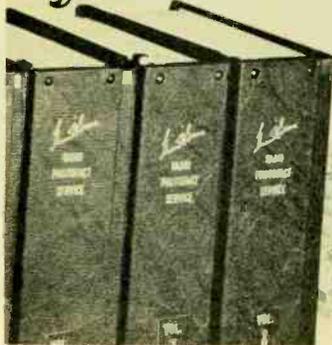
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- VOL. 7—May 1, 1949—Oct. 1, 1949
- VOL. 8—Oct. 1, 1949—Dec. 1, 1949
- VOL. 9—Dec. 1, 1949—Mar. 31, 1950
- VOL. 10—Mar. 31, 1950—July 31, 1950
- VOL. 11—July 31, 1950—Oct. 31, 1950
- VOL. 12—Oct. 31, 1950—Jan. 1, 1951
- VOL. 13—Jan. 1, 1951—Apr. 30, 1951
- VOL. 14—Apr. 30, 1951—Aug. 1, 1951
- VOL. 15—Aug. 1, 1951—Oct. 31, 1951
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- VOL. 17—Jan. 31, 1952—Apr. 30, 1952
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CT-1 48-1	Chassis 20V1 Tel. Rec. (Also see PCB 15—Set 126-1 and PCB 26—Set 146-1) 117-2	Models 4H155A, B Tel. Rec. (See Ch. 20B1)	Models 7C63, 7C63-UL (See Ch. 7C1)	Model 26R35A Tel. Rec. (See Ch. 21B1)
ADMIRAL (Also see Record Change Listing)	Chassis 20X1, 20Y1 Tel. Rec. (Set 110-1) 100-1	Models 4H155S, SN (See Ch. 30B1)	Model 7C63A (See Ch. 7C1)	Model 26R36 Tel. Rec. (See Ch. 24H1)
Chassis L15K1 30-1	Chassis 21A1 Tel. Rec. (Also see PCB 23—Set 140-1) 77-1	Models 4H156A, B Tel. Rec. (See Ch. 20B1)	Models 7C65B, 7C65M, 7C65W (See Ch. 7E1)	Model 26R36A Tel. Rec. (See Ch. 21B1)
Chassis L17C1 25-2	Chassis 21B1 Tel. Rec. (Also see PCB 25—Set 144-1 and PCB 79—Set 220-1) 118-2	Models 4H156S, SN Tel. Rec. (See Ch. 20B1)	Model 7C73 (See Ch. 9A1)	Model 26R37 Tel. Rec. (See Ch. 24H1)
Chassis 3A1 2-24	Chassis 21C1, 21D1 Tel. Rec. (Also see PCB 25—Set 144-1) 118-2	Models 4H157A, B Tel. Rec. (See Ch. 20B1)	Models 7C73, 7C74, 7G15, 7G16 (See Ch. 7G1)	Model 26R37A Tel. Rec. (See Ch. 21B1)
Chassis 3C1 (Also see PCB 15—Set 126-1) 117-2	Chassis 21E1 (See Ch. 21D1—Set 118-2 and PCB 25—Set 144-1) 118-2	Models 4H157S, SN Tel. Rec. (See Ch. 20B1)	Models 7P32, 7P33, 7P34, 7P35 (See Ch. 5H1)	Models 26X35, 26X36 Tel. Rec. (See Ch. 24D1)
Chassis 4A1 3-31	Chassis 21F1, 21G1 Tel. Rec. (Also see PCB 30—Set 156-2 and PCB 46—Set 180-1) 135-2	Models 4H165A, B Tel. Rec. (See Ch. 20B1)	Models 7RT41, 7RT42, 7RT43 (See Ch. 6L1)	Models 26X35A, 26X36A, 26X37A Tel. Rec. (See Ch. 24D1)
Chassis 4B1 24-1	Chassis 21H1, 21J1 Tel. Rec. (Also see PCB 25—Set 144-1) 118-2	Models 4H165S, SN Tel. Rec. (See Ch. 20B1)	Model 7T01 (See Ch. 5N1)	Model 26X37 Tel. Rec. (See Ch. 24D1)
Chassis 4D1 49-1	Chassis 21K1, 21L1 Tel. Rec. (Also see PCB 46—Set 180-1) 135-2	Models 4H166A, B, C, CN Tel. Rec. (See Ch. 20B1)	Model 7T04-UL (See Ch. 5N1)	Model 26X45, 26X46 Tel. Rec. (See Ch. 24H1)
Chassis 4H1 71-2	Chassis 21M1, 21N1 Tel. Rec. (See PCB 30—Set 156-2 and PCB 46—Set 180-1) 135-2	Models 4H166S, SN Tel. Rec. (See Ch. 20B1)	Model 7T06 (See Ch. 4B1)	Models 26X55, 26X56, 26X57 Tel. Rec. (See Ch. 24D1)
Chassis 4J1, 4K1 77-7	Chassis 21P1, 21Q1 Tel. Rec. (Also see PCB 30—Set 156-2 and PCB 46—Set 180-1) 135-2	Models 4H167A, B, C, CN Tel. Rec. (See Ch. 20B1)	Model 7T10 (See Ch. 5K1)	Models 26X55A, 26X56A, 26X57A Tel. Rec. (See Ch. 21D1)
Chassis 4L1 100-1	Chassis 21R1, 21S1 Tel. Rec. (Also see PCB 30—Set 156-2 and PCB 46—Set 180-1) 135-2	Models 4H167S, SN Tel. Rec. (See Ch. 20B1)	Model 7T12 (See Ch. 4B1)	Models 26X65, 26X66, 26X67 Tel. Rec. (See Ch. 24D1)
Chassis 4R1 108-3	Chassis 21T1, 21U1 Tel. Rec. (Set 196-1 and Ch. 21W1—Set 177-2) 177-2	Models 4R11, 4R12 (See Ch. 4R1)	Models 7T14, 7T15 (See Ch. 5K1)	Models 26X65, 26X66, 26X67 Tel. Rec. (See Ch. 24D1)
Chassis 4S1 100-1	Chassis 21V1, 21Z1A Tel. Rec. (Set 196-1 and Ch. 21W1—Set 177-2) 177-2	Model 4T11 (See Ch. 4T1)	Models 8C11, 8C12, 8C13 Tel. Rec. (See Ch. 30A1 and Ch. 8C1)	Models 26X65, 26X66, 26X67 Tel. Rec. (See Ch. 24D1)
Chassis 4T1 143-2	Chassis 21Z1, 21Z1A Tel. Rec. (Set 196-1 and Ch. 21W1—Set 177-2) 177-2	Models 4W18, 4W19 (See Ch. 4W1)	Models 8C14, 8C15, 8C16, 8C17 (See Ch. 8C1)	Models 26X65, 26X66, 26X67 Tel. Rec. (See Ch. 24D1)
Chassis 4W1 143-2	Chassis 22A2, 22A2A Tel. Rec. (Set 180-2) 201-2	Models 5A32/12, 5A32/15, 5A32/16, 5A33/12, 5A33/15, 5A33/16 (See Ch. 5A3)	Models 8D15, 8D16 (See Ch. 8D1)	Models 26X65, 26X66, 26X67 Tel. Rec. (See Ch. 24D1)
Chassis 4A3 191-2	Chassis 22C2 Tel. Rec. (Set 180-2) 201-2	Models 5E21, 5E22, 5E23 (See Ch. 5E2)	Model 8RP46 (See Ch. 3A1)	Models 26X65, 26X66, 26X67 Tel. Rec. (See Ch. 24D1)
Chassis 2B1 (See Model 6T02—Set 1-20) 4-24	Chassis 22E2 Tel. Rec. (Set 180-2) 201-2	Models 5E31, 5E32, 5E33 (See Ch. 5E3)	Models 9B14, 9B15, 9B16 (See Ch. 9B1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5B1A 18-1	Chassis 22F2 Tel. Rec. (Set 180-2) 222-2	Models 5F11, 5F12 (See Ch. 5F1)	Models 9E15, 9E16, 9E17 (See Ch. 9E1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5B2 100-1	Chassis 22G2 Tel. Rec. (Set 180-2) 222-2	Models 5G21, 5G21/15, 5G22, 5G22/5, 5G23, 5G23/15 (See Ch. 5G2)	Models 12X11, 12X12 Tel. Rec. (See Ch. 20Z1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5C3 197-2	Chassis 22H2 Tel. Rec. (Set 180-2) 222-2	Models 5J21, 5J22, 5J23 (See Ch. 5J2)	Models 14R11, 14R12 Tel. Rec. (See Ch. 20T1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5D2 118-2	Chassis 22I2 Tel. Rec. (Set 180-2) 222-2	Models 5K11, 5K12, 5K13, 5K14 (See Ch. 5K1)	Model 14R16 Tel. Rec. (See Ch. 20T1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5E2 139-2	Chassis 22J2 Tel. Rec. (Set 180-2) 222-2	Models 5L21, 5L22, 5L23 (See Ch. 5L2)	Model 15K21 Tel. Rec. (See Ch. 20T1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5E3 224-2	Chassis 22K2 Tel. Rec. (Set 180-2) 222-2	Models 5M21, 5M22 (See Ch. 5M2)	Model 16M12 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5F1 57-1	Chassis 22L2 Tel. Rec. (Set 180-2) 222-2	Model 5R10 (See Ch. 5R1)	Models 16R11, 16R12 Tel. Rec. (See Ch. 21B1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5G2 137-2	Chassis 22M2 Tel. Rec. (Set 180-2) 222-2	Models 5R11, 5R12, 5R13, 5R14 (See Ch. 5R1)	Model 17D10, 17D11, 17D12 Tel. Rec. (See Ch. 19B1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5H1 26-1	Chassis 22N2 Tel. Rec. (Set 180-2) 222-2	Model 5S22AN (See Ch. 5C3)	Models 17K11, 17K12 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5J2 136-2	Chassis 22O2 Tel. Rec. (Set 180-2) 222-2	Model 5S23AN (See Ch. 5C3)	Model 17K16 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5K1 30-1	Chassis 22P2 Tel. Rec. (Set 180-2) 222-2	Model 5T12 (Ch. 5T1)	Models 17K21, 17K22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5L2 160-1	Chassis 22Q2 Tel. Rec. (Set 180-2) 222-2	Models 5W11, 5W12 (See Ch. 5W1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5M2 157-2	Chassis 22R2 Tel. Rec. (Set 180-2) 222-2	Models 5X11, 5X12, 5X13, 5X14 (See Ch. 5X1)	Model 17X16 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5N1 31-1	Chassis 22S2 Tel. Rec. (Set 180-2) 222-2	Models 5X21, 5X22, 5X23 (See Ch. 5X2)	Model 17X17, 17X18 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5R1 59-1	Chassis 22T2 Tel. Rec. (Set 180-2) 222-2	Models 5Y22 (See Ch. 5Y2)	Model 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5R2 165-3	Chassis 22U2 Tel. Rec. (Set 180-2) 222-2	Models 6A21, 6A22, 6A23 (See Ch. 6A2)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5T1 68-1	Chassis 22V2 Tel. Rec. (Set 180-2) 222-2	Model 6C11 (See Ch. 6C1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5W1 79-2	Chassis 22W2 Tel. Rec. (Set 180-2) 222-2	Model 6C71 (See Ch. 10A1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5X1 76-3	Chassis 22X2 Tel. Rec. (Set 180-2) 222-2	Models 6J21, 6J22 (See Ch. 6J2)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5X2 204-2	Chassis 22Y2 Tel. Rec. (Set 180-2) 222-2	Model 6M22 (See Ch. 6M2)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5Y2 188-2	Chassis 22Z2 Tel. Rec. (Set 180-2) 222-2	Models 6N25, 6N26, 6N27 (See Ch. 6N2)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5A1 (See Model 6T01—Set 1-19) 103-1	Chassis 23A1 Tel. Rec. (Set 180-2) 222-2	Model 6Q11 (See Ch. 6Q1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5A2 103-1	Chassis 24D1, 24E1, 24F1, 24G1, 24H1 Tel. Rec. (Also see PCB 9—Set 114-1) 103-2	Model 6R11 (See Ch. 6R1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5B1 48-2	Chassis 30A1 Tel. Rec. (Set 180-2) 57-2	Model 6RP48, 6RP49, 6RP50 (See Ch. 5A1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5C1 53-1	Chassis 30B1, 30C1, 30D1 Tel. Rec. (Set 180-2) 71-2	Models 6S11, 6S12 (See Ch. 6S1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5E1, 6E1N 6-1	Models T1811, T1812 Tel. Rec. (See Ch. 19B1)	Model 6T11 (See Ch. 6T1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5J2 140-2	Model T1822 Tel. Rec. (See Ch. 19B1)	Model 6U11 (See Ch. 6U1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5L1 26-2	Model T2212 Tel. Rec. (See Ch. 19F1A)	Models 6V11, 6V12 (See Ch. 6V1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 5M1 25-1	Model T2222 Tel. Rec. (See Ch. 19F1A)	Model 6W21, 6W12 (See Ch. 6W1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 6M2 (See Ch. 6J2—Set 140-2) 78-1	Model T2226 Tel. Rec. (See Ch. 19F1)	Models 6X21, 6X22, 6X23 (See Ch. 6X2)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 6Q1 54-1	Models 4H15, 4H16, 4H17 (A or B) Tel. Rec. (See Ch. 20A1)	Model 6Y22 (See Ch. 6Y2)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 6S1 107-1	Models 4H15, 4H16, 4H17, 4H18, 4H19 (S or SN) Tel. Rec. (See Ch. 30B1)	Model 6Z11 (See Ch. 6Z1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 6V1 62-1	Models 4H18, 4H19 (C or CN) Tel. Rec. (See Ch. 20B1)	Models 6A11, 6A12, 6A13 (See Ch. 6A1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 6W1 71-1	Models 4H115, 4H116, 4H117 (S or SN) Tel. Rec. (See Ch. 30B1)	Models 6B21, 6B22 (See Ch. 6B2)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 6Y1 75-1	Models 4H126A, B, C, CN Tel. Rec. (See Ch. 21A1)	Models 6C11, 6C12, 6C13, 6C14 (See Ch. 6C1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 7B1 18-2	Model 4H126 (S or SN) Tel. Rec. (See Ch. 30B1)	Models 6D11, 6D12, 6D13, 6D14 (See Ch. 6D1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 7C1 25-2	Models 4H137A, B, C, CN Tel. Rec. (See Ch. 21A1)	Models 6E11, 6E12, 6E13, 6E14 (See Ch. 6E1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 7E1 36-1	Model 4H137 (S or SN) Tel. Rec. (See Ch. 30B1)	Models 6F11, 6F12, 6F13, 6F14 (See Ch. 6F1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 7G1 54-2	Models 4H145A, B, C, CN Tel. Rec. (See Ch. 20B1)	Models 6G11, 6G12, 6G13, 6G14 (See Ch. 6G1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 8C1 (See Ch. 8D1—Set 67-1) 67-1	Models 4H145S, SN Tel. Rec. (See Ch. 30B1)	Models 6H11, 6H12, 6H13, 6H14 (See Ch. 6H1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 8D1 67-1	Models 4H146A, B, C Tel. Rec. (See Ch. 20B1)	Models 6I11, 6I12, 6I13, 6I14 (See Ch. 6I1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 9A1 32-1	Models 4H146S, SN Tel. Rec. (See Ch. 30B1)	Models 6J11, 6J12, 6J13, 6J14 (See Ch. 6J1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 9B1 49-2	Models 4H147A, B Tel. Rec. (See Ch. 20B1)	Models 6K11, 6K12, 6K13, 6K14 (See Ch. 6K1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 9E1 68-2	Models 4H147S, SN Tel. Rec. (See Ch. 30B1)	Models 6L11, 6L12, 6L13, 6L14 (See Ch. 6L1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 10A1 3-30	Models 4H147S, SN Tel. Rec. (See Ch. 30B1)	Models 6M11, 6M12, 6M13, 6M14 (See Ch. 6M1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 19A1 Tel. Rec. (Also see PCB 5—Set 106-1) 59-2	Models 4H147S, SN Tel. Rec. (See Ch. 30B1)	Models 6N11, 6N12, 6N13, 6N14 (See Ch. 6N1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 19B1, 19C1 Tel. Rec. (See Ch. 21A1) 210-2	Models 4H147S, SN Tel. Rec. (See Ch. 30B1)	Models 6O11, 6O12, 6O13, 6O14 (See Ch. 6O1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 19E1 Tel. Rec. (Also see PCB 78—Set 219-1) 203-2	Models 4H147S, SN Tel. Rec. (See Ch. 30B1)	Models 6P11, 6P12, 6P13, 6P14 (See Ch. 6P1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 19F1, 19F1A Tel. Rec. (See Ch. 21A1) 210-2	Models 4H147S, SN Tel. Rec. (See Ch. 30B1)	Models 6Q11, 6Q12, 6Q13, 6Q14 (See Ch. 6Q1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 19G1 Tel. Rec. (See PCB 78—Set 219-1 and Ch. 19E1—Set 203-1) 203-1	Models 4H147S, SN Tel. Rec. (See Ch. 30B1)	Models 6R11, 6R12, 6R13, 6R14 (See Ch. 6R1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 19H1, 19K1 Tel. Rec. (See Ch. 21A1) 210-2	Models 4H147S, SN Tel. Rec. (See Ch. 30B1)	Models 6S11, 6S12, 6S13, 6S14 (See Ch. 6S1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 19N1 Tel. Rec. (See PCB 78—Set 219-1 and Ch. 19E1—Set 203-2) 203-2	Models 4H147S, SN Tel. Rec. (See Ch. 30B1)	Models 6T11, 6T12, 6T13, 6T14 (See Ch. 6T1)	Models 17X21, 17X22 Tel. Rec. (See Ch. 21F1)	Models 26X75A, 26X76A Tel. Rec. (See Ch. 24D1)
Chassis 20A1, 20B1 Tel. Rec. (Also see PCB 23—Set 140-1) 77-1	Models 4H147S, SN Tel. Rec. (See Ch. 30B1)	Models 6U11, 6U12, 6U13, 6U14 (See Ch. 6U1)	Models 17X21, 17X2	

ADMIRAL—AIRLINE

ADMIRAL—Cont.

Models 37F27, A, B, 37F28, A, B Tel. Rec. (See Ch. 21G1 or 21Q1 and Ch. 5D2)	Models 37F35, A, B, 37F36, A, B Tel. Rec. (See Ch. 21G1 or 21Q1 and Ch. 5D2)	Models 37F55, 37F56, 37F67 Tel. Rec. (See Ch. 21G1 or 21Q1 and Ch. 5D2)	Models 37K15, A, B, 37K16, A, B Tel. Rec. (See Ch. 21G1 or 21Q1 and Ch. 3C1)	Models 37K27, A, B, 37K28, A, B Tel. Rec. (See Ch. 21G1 or 21Q1 and Ch. 3C1)	Models 37K35, A, B, 37K36, A, B Tel. Rec. (See Ch. 21G1 or 21Q1 and Ch. 3C1)	Models 37K55, 37K56, 37K57 Tel. Rec. (See Ch. 21G1 or 21Q1 and Ch. 3C1)	Models 37M15, 37M16 Tel. Rec. (See Ch. 21G1 or 21Q1 and Ch. 3C1)	Models 37M25, 37M26, 37M27 Tel. Rec. (See Ch. 21J1)	Models 39X16, A, 39X17, A Tel. Rec. (See Ch. 24G1 and Ch. 5B2) Models 39X18, 39X17B Tel. Rec. (See Ch. 24G1 and Ch. 5D2)	Model 39X17C Tel. Rec. (See Ch. 21J1)	Models 39X25, 39X26 Tel. Rec. (See Ch. 24F and Ch. 5D2)	Models 39X25A, 39X26A Tel. Rec. (See Ch. 21J1)	Models 39X35, 39X36, 39X37 Tel. Rec. (See Ch. 21J1 and Ch. 3C1)	Models 47M15, A, 47M16, 47M17 Tel. Rec. (See Ch. 21W1)	Models 47M35, 47M36, 47M37 Tel. Rec. (See Ch. 21W1)	Models 52M15, 52M16, 52M17 Tel. Rec. (See Ch. 21Y1)	Models 57M10, 57M11, 57M12 Tel. Rec. (See Ch. 21Z1A)	Model 121DX10 Tel. Rec. (See Ch. 19C1)	Model 121DX11 Tel. Rec. (See Ch. 19F1A)	Model 121DX12 Tel. Rec. (See Ch. 19C1)	Model 121DX12A Tel. Rec. (See Ch. 19C1 or 19F1)	Model 121DX16 Tel. Rec. (See Ch. 19C1)	Model 121DX16A Tel. Rec. (See Ch. 19C1 or 19F1)	Model 121DX16L Tel. Rec. (See Ch. 19K1)	Model 121DX17 Tel. Rec. (See Ch. 19C1)	Model 121DX17A Tel. Rec. (See Ch. 19C1 or 19F1)	Model 121DX17L Tel. Rec. (See Ch. 19K1)	Models 121K15, 121K16, 121K17 Tel. Rec. (See Ch. 21M1)	Models 121K15A, 121K16A, 121K17A Tel. Rec. (See Ch. 22M1)	Model 121M10 Tel. Rec. (See Ch. 22A1)	Models 121M11, 121M12 Tel. Rec. (See Ch. 21M1)	Models 121M11A, 121M12A Tel. Rec. (See Ch. 22M1)	Model 122DX12 Tel. Rec. (See Ch. 22F2)	Model 221DX15 Tel. Rec. (See Ch. 19C1)	Model 221DX15A Tel. Rec. (See Ch. 19C1 or 19F1)	Model 221DX15L Tel. Rec. (See Ch. 19K1)	Model 221DX16 Tel. Rec. (See Ch. 19C1)	Model 221DX16A Tel. Rec. (See Ch. 19C1 or 19F1)	Model 221DX16L Tel. Rec. (See Ch. 19K1)	Model 221DX17 Tel. Rec. (See Ch. 19C1)	Model 221DX17A Tel. Rec. (See Ch. 19C1 or 19F1)	Model 221DX17L Tel. Rec. (See Ch. 19K1)	Model 221DX26 Tel. Rec. (See Ch. 19C1)	Model 221DX26A Tel. Rec. (See Ch. 19F1)	Model 221DX26L Tel. Rec. (See Ch. 19K1)	Model 221DX38 Tel. Rec. (See Ch. 19C1)	Model 221DX38A Tel. Rec. (See Ch. 19C1 or 19F1)	Models 221K16, A Tel. Rec. (See Ch. 21K1)	Model 221K26 Tel. Rec. (See Ch. 21K1)	Model 221K28 Tel. Rec. (See Ch. 21K1)	Models 221K35, 221K36 Tel. Rec. (See Ch. 21K1)	Models 221K45, 221K46, 221K47 Tel. Rec. (See Ch. 21M1)	Models 221K45A, 221K46A, 221K47A Tel. Rec. (See Ch. 22M1)	Models 221M26, 221M27 Tel. Rec. (See Ch. 21K1)	Model 222DX15 Tel. Rec. (See Ch. 19H1)	Model 222DX15L Tel. Rec. (See Ch. 22C2)	Model 222DX16 Tel. Rec. (See Ch. 22C2)	Model 222DX16B Tel. Rec. (See Ch. 22M2)	Model 222DX17 Tel. Rec. (See Ch. 22C2)	Model 222DX17B Tel. Rec. (See Ch. 22M2)	Models 222DX26, 222DX27 Tel. Rec. (See Ch. 22C2)
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ADMIRAL—Cont.

Model 222DX27B Tel. Rec. (See Ch. 22M2)	Models 222DX48, 222DX49 Tel. Rec. (See Ch. 22C2)	Models 228DX16, 228DX17 Tel. Rec. (See Ch. 23A1)	Model 320R17 Tel. Rec. (See Ch. 21J1)	Models 320R25, 320R26 Tel. Rec. (See Ch. 21J1)	Models 321DX15, 321DX16, 321DX17 Tel. Rec. (See Ch. 19E1)	Models 321DX15A, 321DX16A, 321DX17A Tel. Rec. (See Ch. 19E1 or Ch. 19G1)	Models 321DX15L, 321DX16L, 321DX17L Tel. Rec. (See Ch. 19N1)	Model 321DX25B Tel. Rec. (See Ch. 19E1 or Ch. 19G1)	Model 321DX26 Tel. Rec. (See Ch. 19E1)	Model 321DX26B Tel. Rec. (See Ch. 19E1 or Ch. 19G1)	Model 321DX27B Tel. Rec. (See Ch. 19E1 or Ch. 19G1)	Models 321F15, 321F16 Tel. Rec. (See Ch. 21L1 and Ch. 5D2)	Model 321F18 Tel. Rec. (See Ch. 21L1 and Ch. 5D2)	Model 321F27 Tel. Rec. (See Ch. 21L1 and Ch. 5D2)	Models 321F35, 321F36 Tel. Rec. (See Ch. 21L1 and Ch. 5D2)	Models 321F46, 321F47 Tel. Rec. (See Ch. 21L1 and Ch. 5D2)	Model 321F49 Tel. Rec. (See Ch. 21L1 and Ch. 5D2)	Models 321F65, 321F66, 321F67 Tel. Rec. (See Ch. 21W1 and Ch. 5D2)	Models 321K15, 321K16 Tel. Rec. (See Ch. 21L1 and Ch. 3C1)	Model 321K18 Tel. Rec. (See Ch. 21L1 and Ch. 3C1)	Model 321K27 Tel. Rec. (See Ch. 21L1 and Ch. 3C1)	Models 321K35, 321K36 Tel. Rec. (See Ch. 21L1 and Ch. 3C1)	Models 321K46, 321K47 Tel. Rec. (See Ch. 21L1 and Ch. 3C1)	Models 321K65, 321K66, 321K67 Tel. Rec. (See Ch. 21N1 and 3C1)	Models 321M25, 321M26, 321M27 Tel. Rec. (See Ch. 21Y1)	Models 321M25A, 321M26A, 321M27A Tel. Rec. (See Ch. 22Y1)	Model 322DX16 Tel. Rec. (See Ch. 22E2)	Model 322DX16A Tel. Rec. (See Ch. 22P2)	Models 421M15, 421M16 Tel. Rec. (See Ch. 21Y1)	Models 421M15A, 421M16A Tel. Rec. (See Ch. 22Y1)	Models 421M35, 421M36, 421M37 Tel. Rec. (See Ch. 22Y1)	Models 520M11, 520M12 Tel. Rec. (See Ch. 22A2A)	Models 520M15, 520M16, 520M17 Tel. Rec. (See Ch. 22A2)	Models 521M15, 521M16, 521M17 Tel. Rec. (See Ch. 21Y1)	Models 521M15A, 521M16A, 521M17A Tel. Rec. (See Ch. 22Y1)
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AERMOTIVE

181-AD 12-1

AERO (See Record Changer Listing)

AIMEE (See AMC)

AIRADIO

AU-41D	11-1
SU-52A, B, C (Receiver)	13-2
TRA-1A, B, C (Transmitter)	13-1
3100	37-1

AIRCATTLE

C-300	136-3
DM-700	85-1
EV-760	48-3
G-516, G-518	54-3
G-521	54-3
G-724	52-25
G-725	50-1
K1	93-1
P-20	71-3
PAM-4	87-1
PAM-4	101-1
PC-8, PC-358	99-1
PM-78	100-2
PM-358	98-1
PX	13-35
REV248	127-2
RZU248 (See Model REV248—Set 127-2)	
SC-448	62-2
TD-6	103-3
WEU-262	91-1
WRA-4A	47-1
WRA-4M	60-1
XB702, XB703 Tel. Rec.	93A-1
XL750, XP775 Tel. Rec.	93A-1
OA-358-VM (See Model 358VM— Set 127-3)	
OF, OF-L	135-3
98	52-1
9	50-2
10C, 10T Tel. Rec. (See Model 14C —Set 140-3)	
12C, 12T Tel. Rec. (See Model 14C —Set 140-3)	
14C, 14T Tel. Rec.	140-3
15	67-2
16C, 16T Tel. Rec. (See Model 14C —Set 140-3)	
17C, 17T Tel. Rec.	140-3
20XUT Tel. Rec.	185-3
79A	137-3
88, 88W	142-2
101	86-1
102B	98-2
1068	13-3

AIRCATTLE—Cont.

150, 153	126-2
171, 172	96-1
198	83-1
200	139-3
201	81-1
211	65-1
212	68-3
221	63-1
221L, 227W	84-1
313 Tel. Rec. (See Model 14C—Set 140-3)	
316 Tel. Rec. (See Model 14C—Set 140-3)	
350	136-4
358VM	127-3
412 Tel. Rec. (See Model 14C—Set 140-3)	
416 Tel. Rec. (See Model 14C—Set 140-3)	
472 JP24, 472 JP25 (See Model 472 MP25—Set 168-1)	
472 MP24 (See Model 472 MP25— Set 168-1)	
472 MP25	168-1
472-053VM	163-2
472-17XUCM, 472-17XUCM.1 (Ch. 317-B) Tel. Rec.	223-2
472-17XUCM.2, 472-17XUCM.3, 472-17XUCM.4, 472-17XUCM.5 (Ch. 317-D) Tel. Rec.	223-2
472-17XUCO, 472-17XUCO.1 (Ch. 317-B) Tel. Rec.	223-2
472-17XUT, 472-17XUT.1, 472- XUT.2, 472-XUT.3 (Ch. 217B) Tel. Rec. (See Model 20XUT—Set 185-3)	
472-17XUT.4, 472-17XUT.5 (Ch. 317-B) Tel. Rec.	223-2
472-17XUT.6, 472-17XUT.7, 472- 17XUT.8 (Ch. 317-D) Tel. Rec.	223-2
472-20XUC (Ch. 220B) Tel. Rec. (See Model 20XUT—Set 185-3)	
472-20XUT, 472-20XUT.1, 472- 20XUT.2 (Ch. 220B) Tel. Rec. (See Model 20XUT—Set 185-3)	
472-21XUCO (Ch. 321-B) Tel. Rec. 472-21XUCO.1, 472-21XUCO.2 (Ch. 321-D) Tel. Rec.	223-2
472-21XUT, 472-21XUT.1 (Ch. 321-B) Tel. Rec.	223-2
472-21XUT.2 (Ch. 321-D) Tel. Rec.	223-2
472-217C, 472-217C.1 (Ch. 317-D) Tel. Rec.	223-2
472-217T, 472-217T.1 (Ch. 317-D) Tel. Rec.	223-2
472-221XC (Ch. 321-D) Tel. Rec.	223-2
472-221XT, 472-221XT.1 (Ch. 321- D) Tel. Rec.	223-2
472-254	213-2
568	14-1
568.205	141-2
568.205-1 (See Model 200—Set 139-3)	
568.305	141-2
572	15-1
594.935 (See Model 935—Set 128-2)	
602-182144	114-2
603-PR-8.1	133-2
603-80	230-2
604	63-8
606-400WB	119-2
607-299	177-3
607-314, 607-315	122-2
607-316, -1, 607-317, -1	138-2
610.667	247-2
610.C351	174-2
610.C1152B, M	208-1
610.D200	142-3
610.FE-153	244-2
610.F100	138-3
610.F151	172-2
610.H400	119-2
610.I.P-651.1	179-2
610.5500	184-2
610.W-100	249-2
621 (Ch. FJ-91)	14-2
626	18-3
641	15-1
651	17-1
652.A25, 652.A35	169-2
652.351	231-2
652.5C1M, V	246-1
652.5T3M, V	246-1
652.6T1E, V	205-2
652.3275A	210-3
652.4875	211-3
652.505	168-2
659.511, 659.513	167-2
659.520E, I	185-4
738.5400, UL	250-2
9151, W	129-2
925	128-2
9651, W, 965K1, W (See Model 9511—Set 129-2)	
1400C, 1400T Tel. Rec.	140-3
1700C, 1700T Tel. Rec.	140-3
2000C Tel. Rec.	140-3
317A Tel. Rec. (For TV Ch. See Set 140-3, For Radio Ch. See Model 350—Set 136-4)	
5000, 5001	16-2
5002	19-1
5003, 5004, 5005, 5006	20-1
5008, 5009	46-1
5010, 5011, 5012 (Ch. 110)	13-4
5015.1	118-3
5020	16-3
5022	123-2
5024	45-1
5025	24-2
5027	49-3
5028	44-1
5029	51-1
5035	46-2
5036	72-2
5044	121-2
5050	48-4

AIRCATTLE—Cont.

5052	45-2
5054	120-2
6042	61-1
6050	74-1
6053	97-1
6514	18-4
6541	17-2
6544 (See Model 6541—Set 84-1)	17-2
6611, 6612, 6613, 6630, 6631, 6632, 6634, 6635	15-2
7000, 7001	14-3
7004	19-2
7014, 7015	57-3
7015 Early	47-2
7553	45-3
90081, 9008W	99-2
90091, 9009W	97-2
90121, 9012W	94-1
10002	54-1
10003-1	46-2
10003-2	62-3
10021-1, 10022-1	59-3
10023	58-1
10024-1	58-2
108014, 108504	73-1
121014	61-2
121015	55-2
127084	60-2
131504	69-1
132564	54-3
138104	64-1
138124	64-1
139114 (See Model 139144—Set 59-4)	
147114	56-3
149654	71-4
150084	71-4
159144 (See Model 139144—Set 59-4)	
Ch. 217B (See Model 472-17XUT Ch. 220B (See Model 472-20XUC) Ch. 317-B (See Model 472-17XUCM) Ch. 317-D (See Model 472-17- XUCM.2) Ch. 321-B (See Model 472-21XUT) Ch. 321-D (See Model 472-21XUT.2)	

AIR CHIEF (See Firestone)

AIR KING

A-400 (Ch. 470)	23-1
A-403	20-2
A-410	34-1
A-410 (Revised)	40-1
A-426	43-1
A-501, A-502 (Ch. 465.4)	24-3
A-510	30-2
A-511, A-512	49-4
A-520	26-3
A-604	81-2
A-625	50-3
A-650	45-4
A-1000, A-1001 Tel. Rec.	58-3
A1001A Tel. Rec.	75-2
A1016 Tel. Rec.	91-2
A2000, A2001 Tel. Rec.	75-2
A2002 Tel. Rec. (See Model A2000 —Set 75-2)	
A2010 Tel. Rec.	75-2
A2012 Tel. Rec. (See Model A1001A —Set 75-2)	
12C1 Tel. Rec. (See Model 16C1— Set 121-3)	
12T1, 12T2 Tel. Rec. (See Model 16C1—Set 121-3)	
14T1 Tel. Rec. (See Model 16C1— Set 121-3)	
16C1, 16C2, 16C5 Tel. Rec.	121-3
16M1 Tel. Rec.	121-3
16T1 Tel. Rec.	121-3
16T1B Tel. Rec. (See Model 16C1— Set 121-3)	
17C2 (Ch. 700-96) Tel. Rec.	151-2
17C5, B (Ch. 700-96) Tel. Rec.	151-2
17C7 (Ch. 700-96) Tel. Rec.	151-2
17K1 (Ch. 700-96) Tel. Rec.	151-2
17K1C (Ch. 700.110, 700.130) Tel. Rec.	150-2
17M1 (Ch. 700-96) Tel. Rec.	151-2
17T1 (Ch. 700-96) Tel. Rec.	151-2
19C1 Tel. Rec.	121-3
20C1, 20C2 (Ch. 700-93) Tel. Rec.	151-2
20K1 (Ch. 700-95) Tel. Rec.	151-2

CENTURY (20th)—CROSLEY

CENTURY (20th)
 100X, 101, 104 12-5
 200 21-5
 300 21-6

CHALLENGER
 CC8 63-4
 CC18 67-7
 CC30 68-6
 CC60 70-3
 CC618 66-4
 CD6 65-4
 20R 69-5
 60R 62-7
 200 69-5
 600 62-7

CHANCELLOR (Also see Radionic)
 35P 30-25

CHEVROLET
 985792 6-5
 985793 19-6
 986067 90-2
 986146 28-6
 986240 75-5
 986241 58-7
 986388 104-5
 986443 189-4
 986515 149-5
 986516 150-6
 986668 219-2
 986669 224-6

CHRYSLER (See Mopar)

CISCO
 1A5 37-4
 9A5 20-3

CLARION
 C100 1-5
 C101 5-9
 C102 9-6
 C103 6-6
 C104 1-4
 C105 (See Model C-104—Set 4) 6-7
 C105A 4-7
 C108 (Ch. 101) 5-8
 11011 17-8
 11305 18-11
 11411-N 30-5
 11801 23-6
 11802V-M (See Model 11801—Set 23-6) 54-5
 12100M 31-6
 12310-W 41-5
 12708 61-5
 12801 46-7
 13101 62-8
 13201, 13203 60-9
 14601 66-5
 14965 102-2
 16703 Tel. Rec. 102-2

CLARK
 PA-10 12-6
 PA-10A 18-12
 PA-20 13-12
 PA-20A 18-13
 PA-30 19-7

CLEARSONIC (See U. S. Television)

COLLINS AUDIO PRODUCTS
 FMA-6 99-6
 45-D 72-6

COLLINS RADIO
 75A-1 34-4
 75A-2 171-4

COLUMBIA RECORDS
 202 219-3
 360 Series 'B' 215-5

COMMANDER INDUSTRIES
 Commander 3 Tube Record Player 17-10
 CD61P 19-9

CONCERTONE (See Recorder Listing)

CONCORD
 IN434, IN435, IN436 (Similar to Chassis) 98-5
 IN437 (Similar to Chassis) 121-2
 IN549 (Similar to Chassis) 38-5
 IN551 (Similar to Chassis) 38-6
 IN554, IN555 (Similar to Chassis) 55-10
 IN556, IN557 (Similar to Chassis) 102-7
 IN559 (Similar to Chassis) 90-7
 IN560 (Similar to Chassis) 109-7
 IN561, IN562 (Similar to Chassis) 97-8
 IN563 (Similar to Chassis) 136-10
 IN819 (Similar to Chassis) 69-7
 6C51B 19-8
 6C51W 19-8
 6E51B 20-4
 6F26W 19-10
 6R3ARC 21-7
 6T61W 22-5
 7G26C 20-5
 7R3APW 21-7
 1-402, 1-403 45-6
 1-411 48-5
 1-501 (See Model 6E51B—Set 20-4) 55-4
 1-504 55-6
 1-509, 1-510 (See Model 6C51B—Set 19-8) 49-7
 1-516, 1-517 49-7
 1-601, 1-602, 1-603 (See Model 7G26C—Set 20-5) 45-7
 1-606 45-7
 1-608 (See Model 6F26W—Set 19-10) 45-6
 1-609 (See Model 6T61W—Set 22-11) 46-8
 1-611 55-7
 1-1201 55-7
 2-105 (See Model 315W1—Set 53-8) 54-6
 2-106 54-6
 2-200, 2-201, 2-218, 2-219, 2-232, 2-235, 2-236, 2-237, 2-238, 2-239, 2-240 62-9
 315W1, 315W2 53-8
 325W1, 325W2 (See Model 2-106—Set 54-6) 183-4

CONRAC
 10-M-36, 10-W-36 (Ch. 36) Tel. Rec. (See Ch. 36) 11-3
 11-B-36 (Ch. 36) Tel. Rec. (See Ch. 36) 12-3
 12-M-36, 12-W-36 (Ch. 36) Tel. Rec. (See Ch. 36) 13-3
 13-B-36 (Ch. 36) Tel. Rec. (See Ch. 36) 14-3
 14-M-36, 14-W-36 (Ch. 36) Tel. Rec. (See Ch. 36) 15-3
 15-P-36 (Ch. 36) Tel. Rec. (See Ch. 36) 16-3
 16-B-36 (Ch. 36) Tel. Rec. (See Ch. 36) 17-3
 17-P-39 (Ch. 39) Tel. Rec. (See Ch. 39) 18-3
 18-M-39, 18-W-39 (Ch. 39) Tel. Rec. (See Ch. 39) 19-3
 20-M-39, 20-W-39 (Ch. 39) Tel. Rec. (See Ch. 39) 21-3
 21-B-39 (Ch. 39) Tel. Rec. (See Ch. 39) 22-3
 22-P-39 (Ch. 39) Tel. Rec. (See Ch. 39) 23-3
 23-M-390, 23-W-390 (Ch. 39) Tel. Rec. (See Ch. 39) 24-3
 24-M-36 (Ch. 36) Tel. Rec. (See Ch. 36) 25-3
 25-W-36 (Ch. 36) Tel. Rec. (See Ch. 36) 26-3
 26-B-36 (Ch. 36) Tel. Rec. (See Ch. 36) 27-3
 27-M-40, 27-W-40 (Ch. 40) Tel. Rec. (See Ch. 40) 28-3
 28-B-40 (Ch. 40) Tel. Rec. (See Ch. 40) 29-3
 29-P-40 (Ch. 40) Tel. Rec. (See Ch. 40) 30-3
 30-M-40, 30-W-40 (Ch. 40) Tel. Rec. (See Ch. 40) 31-3
 31-P-40 (Ch. 40) Tel. Rec. (See Ch. 40) 32-3
 32-M-44, 32-W-44 (Ch. 44) Tel. Rec. (See Ch. 44) 33-3
 33-B-44 (Ch. 44) Tel. Rec. (See Ch. 44) 34-3
 34-P-44 (Ch. 44) Tel. Rec. (See Ch. 44) 35-3
 35-M-61, 35-W-61 (Ch. 61) Tel. Rec. (See Ch. 61) 36-3
 36-B-61 (Ch. 61) Tel. Rec. (See Ch. 61) 37-3
 37-P-61 (Ch. 61) Tel. Rec. (See Ch. 61) 38-3
 38-B-61, 38-W-61 (Ch. 61) Tel. Rec. (See Ch. 61) 39-3
 39-M-61 (Ch. 61) Tel. Rec. (See Ch. 61) 40-3
 40-M-64, 40-W-64 (Ch. 64) Tel. Rec. (See Ch. 64) 41-3
 41-B-64 (Ch. 64) Tel. Rec. (See Ch. 64) 42-3
 42-P-64 (Ch. 64) Tel. Rec. (See Ch. 64) 43-3
 43-B-64, 43-M-64 (Ch. 64) Tel. Rec. (See Ch. 64) 44-3
 Ch. 36 Tel. Rec. 110-4
 Ch. 39 Tel. Rec. 110-4
 Ch. 40 Series Tel. Rec. 140-4
 Ch. 44 Tel. Rec. (See PCB 27—Set 148-1 and Ch. 40—Set 140-4) 185-5
 Ch. 61, 64 Series Tel. Rec. 185-5

CONTINENTAL ELECTRONICS (See Skyweight)

CONVERSA-PONE
 MS-5 (Master Station) SS-5 (Sub-Station) 16-7

CO-OP
 6AWC, 6AWC3, 6A47WCR, 6A47-WT, 6A47WTR 8-8

CORONADO
 FA43-8965 Tel. Rec. (See Model 43-8965—Set 86-3) 182-3
 K-21 (43-9041) Tel. Rec. 182-3
 K-72 (43-9031) Tel. Rec. 182-3
 K-73L (43-9030) Tel. Rec. 182-3
 RA37-43-9855 227-5
 OSRA1-43-7755A, OSRA1-43-7755B 21-2
 OSRA1-43-7901A 115-2
 OSRA2-43-8230A 162-3
 OSRA2-43-8515A 110-5
 OSRA4-43-9876A 103-7
 OSRA33-43-8120A 110-6
 OSRA33-43-8135 140-4
 94RA33-43-8130C—Set 82-3 102-2
 OSRA37-43-8360A 102-3
 OSTV1-43-8945A Tel. Rec. 145-5
 OSTV1-43-9005A, OSTV1-43-9006A Tel. Rec. 145-5
 OSTV1-43-9014A Tel. Rec. 128-4
 OSTV2-43-8950A Tel. Rec. 141-4
 OSTV2-43-9010A Tel. Rec. 146-5
 OSTV2-43-9010B Tel. Rec. 153-2
 15RA1-43-7654A 147-3
 15RA1-43-7902A 134-6
 15RA2-43-8230A 162-3
 15RA4-43-9876C, 15RA4-43-9877 (See Model OSRA4-43-9876A—Set 103-7) 174-5
 15RA33-43-8245A, 15RA33-43-8246A 174-5
 15RA33-43-8365 169-4
 15RA37-43-9230A 173-5
 15TV1-43-8957A, B Tel. Rec. (Also see PCB 34—Set 162-1) 161-3
 15TV1-43-9008A Tel. Rec. 162-4
 15TV1-43-9015A, B, 15TV1-43-9016A, B Tel. Rec. (Also see PCB 34—Set 162-1) 161-3
 15TV1-43-9020A, B, 15TV1-43-9021A, B Tel. Rec. (Also see PCB 34—Set 162-1) 161-3
 15TV2-43-9012A, 15TV2-43-9013A Tel. Rec. 152-4
 15TV2-43-9025A, B, 15TV2-43-9026A, B Tel. Rec. 144-3
 15TV2-43-9101A, 15TV2-43-9102A Tel. Rec. 152-4
 15TV4-43-8948A, 15TV4-43-8949A Tel. Rec. 175-7
 25TV2-43-9022A Tel. Rec. 183-4

CORONADO—Cont.
 25TV2-43-9022B Tel. Rec. (See PCB 65—Set 202-1 and Model 25TV2-43-9022A—Set 183-4) 214-3
 25TV2-43-9022C Tel. Rec. (See PCB 65—Set 202-1, PCB 72—Set 212-1 and Model 25TV2-43-9022A—Set 183-4) 219-5
 25TV2-43-9045A, B Tel. Rec. 199-5
 25TV2-43-9045C Tel. Rec. (See PCB 68—Set 205-1 and Model 25TV2-43-9045A—Set 199-5) 219-5
 25TV2-43-9050A Tel. Rec. 199-5
 25TV2-43-9060B Tel. Rec. (See PCB 68—Set 205-1 and Model 25TV2-43-9060A—Set 199-5) 214-3
 35RA4-43-8566A 221-4
 35RA33-43-8125 217-5
 35RA33-43-8145 224-7
 35RA33-43-8225 219-4
 35RA37-43-8355 225-9
 35RA40-43-8247A 236-3
 35TV2-43-9022C Tel. Rec. (See PCB 65—Set 202-1, PCB 72—Set 212-1 and Model 25TV2-43-9022A—Set 183-4) 219-5
 35TV2-43-9023A Tel. Rec. 234-4
 35TV2-43-9045D Tel. Rec. (See PCB 68—Set 205-1, PCB 71—Set 211-1 and Model 25TV2-43-9045E Tel. Rec. (See Model 35TV2-43-9045D) 237-5
 35TV2-43-9060C Tel. Rec. (See PCB 66—Set 205-1, PCB 71—Set 211-1 and Model 25TV2-43-9060A—Set 199-5) 7-4
 35TV2-43-9060D Tel. Rec. (See Model 35TV2-43-9060C) 237-5
 35TV2-43-9061A Tel. Rec. 237-5
 43-2027 11-3
 43-5005 28-36
 43-6011 7-4
 43-6451 10-10
 43-6485 46-9
 43-6730 (See Model 43-8685—Set 11-4) 10-11
 43-7601 (See Model 43-7601B—Set 10-11) 9-7
 43-7602 (See Model 43-7601B—Set 10-11) 9-7
 43-7652 (See Model 43-7651—Set 9-7) 47-5
 43-7851 47-5
 43-7852 (See Model 43-7851—Set 47-5) 8-3
 43-8101 (See Model 94RA31-43-8115A—Set 81-5) 82-3
 43-8102, 43-8130C (See Model 94RA33-43-8130C—Set 82-3) 12-7
 43-8160 12-7
 43-8177 (See Model 43-8178—Set 21-8) 21-8
 43-8178 21-8
 43-8180 10-12
 43-8190 19-11
 43-8201 (See Model 43-8178—Set 21-8) 7-5
 43-8213 12-8
 43-8240, 43-8241 8-3
 43-8305 8-3
 43-8312A 19-12
 43-8330 12-9
 43-8351, 43-8352 12-9
 43-8353, 43-8354 28-7
 43-8420 24-13
 43-8470 8-3
 43-8471 9-8
 43-8576B 9-8
 43-8685 11-4
 43-8965 Tel. Rec. 86-3
 43-9030 Tel. Rec. 182-3
 43-9031 Tel. Rec. 182-3
 43-9032 Tel. Rec. 182-3
 43-9196 14-35
 43-9201 24-14
 43-9841A (See Model 94RA31-43-9841A—Set 79-3) 232-3
 45RA1-43-7666A, 45RA1-43-7911A (See Model 15RA1-43-7902A—Set 134-6) 224-7
 45RA33-43-8126 (See Model 35RA33-43-8125—Set 217-5) 224-7
 45RA33-43-8146 (See Model 35RA33-43-8145—Set 224-7) 82-26
 45RA33-43-8225, 45RA33-43-8226, 45RA33-43-8227, 45RA33-43-8228 (See Model 35RA33-43-8225—Set 219-4) 225-9
 45RA37-43-8355 (See Model 35RA37-43-8356—Set 225-9) 234-4
 45TV2-43-9023B Tel. Rec. 234-4
 45TV2-43-9045F Tel. Rec. (See Model 35TV2-43-9045D) 237-5
 45TV2-43-9050B Tel. Rec. (See Model 35TV2-43-9050A—Set 237-5) 237-5
 45TV2-43-9060E Tel. Rec. (See Model 35TV2-43-9045D) 237-5
 45TV2-43-9061B Tel. Rec. 237-5
 45TV2-43-9064A Tel. Rec. 237-5
 94RA1-43-6945A 69-6
 94RA1-43-7605A 65-5
 94RA1-43-7656A, 94RA1-43-7657A 73-2
 94RA1-43-7751A 87-3
 94RA1-43-8510A, 94RA1-43-8511A 71-7
 94RA1-43-8510B, 94RA1-43-8511B 75-6
 94RA2-43-8230A 162-3
 94RA4-43-8129A, 94RA4-43-8130A, 94RA4-43-8130B, 94RA4-43-8131, 94RA4-43-8131B, 94RA4-43-8132A (See Model 94RA4-43-8129A—Set 62-10) 81-5
 94RA31-43-8115A, B, 94RA31-43-8116A 81-5
 94RA31-43-9841A 79-3
 94RA33-43-8130C, 94RA33-43-8131C 82-3

CORONADO—Cont.
 94TV2-43-8970A, 94TV2-43-8971A, 94TV2-43-8972A, 94TV2-43-8973A, 94TV2-43-8985A, 94TV2-43-8986A, 94TV2-43-8987A, 94TV2-43-8993A, 94TV2-43-8994A, 94TV2-43-8995A Tel. Rec. 78-4
 94TV6-43-8953A Tel. Rec. 106-3
 165 (See Model 94RA31-43-8115A—Set 81-5) 197, U (See Model 94RA31-43-8115A—Set 81-5) 2027 (See Model 43-2027—Set 11-3) 5005 (See Model 43-5005—Set 28-36) 5101A (See Model 35RA2-43-5101A—Set 214-3) 6301 (See Model 43-6301—Set 7-4) 6451 (See Model 43-6451—Set 10-10) 6485 (See Model 43-6485—Set 46-9) 6730 (See Model 43-8685—Set 11-4) 6945A (See Model 94RA1-43-6945A—Set 69-6) 7601, B, 7602 (See Model 43-7601B—Set 10-11) 7605A (See Model 94RA1-43-7605A—Set 65-5) 7651, 7652 (See Model 43-7651—Set 9-7) 7654A (See Model 15RA1-43-7654A—Set 147-3) 7656A, 7657A (See Model 94RA1-43-7656A—Set 73-2) 7666A (See Model 45RA1-43-7666A—Set 232-3) 7751 (See Model 94RA1-43-7751A—Set 87-3) 7755A, B (See Model OSRA1-43-7755A—Set 101-2) 7851 (See Model 43-7851—Set 47-5) 7901A (See Model OSRA1-43-7901A—Set 115-2) 7902A (See Model 15RA1-43-7902A—Set 134-6) 7910A, 7911A (See Model 15RA1-43-7902A—Set 134-6) 8101 (See Model 94RA31-43-8115A—Set 81-5) 8115A, B, 8116A (See Model 94RA31-43-8115A—Set 81-5) 8120A (See Model OSRA33-43-8120A—Set 110-6) 8125 (See Model 35RA33-43-8125—Set 217-5) 8129A, 8130A, B, 8131A, B (See Model 94RA-43-8129A—Set 62-10) 8130C, 8131C (See Model 94RA33-43-8130C—Set 82-3) 8145 (See Model 35RA33-43-8145—Set 224-7) 8160 (See Model 43-8160—Set 12-7) 8177, 8178 (See Model 43-8178—Set 21-8) 8180 (See Model 43-8180—Set 10-12) 8190 (See Model 43-8190—Set 19-11) 8201 (See Model 43-8178—Set 21-8) 8213 (See Model 43-8213—Set 7-5) 8225 (See Model 35RA33-43-8225—Set 219-4) 8230A (See Model OSRA2-43-8230A—Set 162-3) 8240, 8241 (See Model 43-8240—Set 12-8) 8245A, 8246A (See Model 15RA33-43-8245A—Set 174-5) 8305 (See Model 43-8305—Set 8-3) 8312A (See Model 43-8312A—Set 8-4) 8330 (See Model 43-8330—Set 19-12) 8351, 8352 (See Model 43-8351—Set 12-9) 8353, 8354 (See Model 43-8353—Set 28-7) 8355 (See Model 35RA37-43-8355—Set 225-9) 8360A (See Model OSRA37-43-8360A—Set 102-3) 8365 (See Model 15RA33-43-8365—Set 69-4) 8420 (See Model 43-8420—Set 24-13) 8470 (See Model 43-8305—Set 8-3) 8471 (See Model 43-8312A—Set 8-4) 8510A, 8511A (See Model 94RA1-43-8510A—Set 71-7) 8510B, 8511B (See Model 94RA1-43-8510B—Set 75-6) 8515 (See Model OSRA2-43-8515A—Set 110-5) 8576B (See Model 43-8576B—Set 9-8) 8685 (See Model 43-8685—Set 11-4) 8945A Tel. Rec. (See Model OSTV1-43-8945A—Set 145-5) 8948A, 8949A Tel. Rec. (See Model 15TV4-43-8948A—Set 175-7) 8950A Tel. Rec. (See Model OSTV2-43-9010A—Set 146-5) 8953A Tel. Rec. (See Model 94TV6-43-8953A—Set 106-3) 8957A Tel. Rec. (See Model 15TV1-43-8957A—Set 62-4) 8958A, B Tel. Rec. (See PCB 34—Set 162-1 and Model 15TV1-43-8958A—Set 161-3) 8965 Tel. Rec. (See Model 43-8965—Set 86-3) 8970A, 8971A, 8972A, 8973A Tel. Rec. (See Model 94TV2-43-8970A—Set 78-4) 8985A, 8986A, 8987A Tel. Rec. (See Model 94TV2-43-8970A—Set 78-4) 8993A, 8994A, 8995A Tel. Rec. (See Model 94TV2-43-8970A—Set 78-4) 9005A, 9006A Tel. Rec. (See Model OSTV1-43-8945A—Set 145-5) 9010A Tel. Rec. (See Model OSTV2-43-9010B—Set 153-2) 9014A Tel. Rec. (See Model OSTV1-43-9014A—Set 128-4) 9015A, B, 9016A, B Tel. Rec. (See Model 15TV1-43-8957A—Set 162-4) 9020A, B, 9021A, B Tel. Rec. (See PCB 34—Set 162-1 and Model 15TV1-43-8958A—Set 161-3) 9022A Tel. Rec. (See Model 25TV2-43-9022A—Set 183-4) 9022B Tel. Rec. (See PCB 65—Set 202-1 and Model 25TV2-43-9022A—Set 183-4) 9022C Tel. Rec. (See PCB 65—Set 205-1 and PCB 72—Set 212-1 and Model 25TV2-43-9022A—Set 183-4) 9025A, B, 9026A, B Tel. Rec. (See Model 15TV2-43-9025A—Set 144-3) 9030 Tel. Rec. (See Model K-73L [43-9031]—Set 182-3) 9031 Tel. Rec. (See Model K-72 [43-9031]—Set 182-3) 9041 (See Model K-21 [43-9041]—Set 182-1) 9045A, B Tel. Rec. (See Model 25TV2-43-9045A—Set 199-5) 9045D, E, F Tel. Rec. (See PCB 68—Set 205-1 and PCB 71—Set 211-1 and Model 25TV2-43-9045A—Set 199-5) 9060A Tel. Rec. (See Model 25TV2-43-9060A—Set 199-5) 9060B Tel. Rec. (See PCB 68—Set 205-1 and Model 25TV2-43-9060A—Set 199-5) 9060C, D, E Tel. Rec. (See PCB 66—Set 205-1, PCB 71—Set 211-1 and Model 25TV2-43-9060A—Set 199-5) 9101, 9102A Tel. Rec. (See Model 15TV2-43-9101A—Set 152-4) 9169 (See Model 43-9169—Set 14-35) 9201 (See Model 43-9201—Set 24-14) 9230A (See Model 15RA37-43-9230A—Set 173-5) 9841A (See Model 94RA31-43-9841A—Set 79-3) 9855 (See Model RA37-43-9855—Set 227-5) 9856A (See Model 35RA4-43-9856A—Set 221-4) 9876A (See Model OSRA4-43-9876A—Set 103-7)

CORONADO—Cont.
 9005A, 9006A Tel. Rec. (See Model OSTV1-43-8945A—Set 145-5) 9010A Tel. Rec. (See Model OSTV2-43-9010B—Set 153-2) 9010B Tel. Rec. (See Model OSTV2-43-9010B—Set 153-2) 9014A Tel. Rec. (See Model OSTV1-43-9014A—Set 128-4) 9015A, B, 9016A, B Tel. Rec. (See Model 15TV1-43-8957A—Set 162-4) 9020A, B, 9021A, B Tel. Rec. (See PCB 34—Set 162-1 and Model 15TV1-43-8958A—Set 161-3) 9022A Tel. Rec. (See Model 25TV2-43-9022A—Set 183-4) 9022B Tel. Rec. (See PCB 65—Set 202-1 and Model 25TV2-43-9022A—Set 183-4) 9022C Tel. Rec. (See PCB 65—Set 205-1 and PCB 72—Set 212-1 and Model 25TV2-43-9022A—Set 183-4) 9025A, B, 9026A, B Tel. Rec. (See Model 15TV2-43-9025A—Set 144-3) 9030 Tel. Rec. (See Model K-73L [43-9031]—Set 182-3) 9031 Tel. Rec. (See Model K-72 [43-9031]—Set 182-3) 9041 (See Model K-21 [43-9041]—Set 182-1) 9045A, B Tel. Rec. (See Model 25TV2-43-9045A—Set 199-5) 9045D, E, F Tel. Rec. (See PCB 68—Set 205-1 and PCB 71—Set 211-1 and Model 25TV2-43-9045A—Set 199-5) 9060A Tel. Rec. (See Model 25TV2-43-9060A—Set 199-5) 9060B Tel. Rec. (See PCB 68—Set 205-1 and Model 25TV2-43-9060A—Set 199-5) 9060C, D, E Tel. Rec. (See PCB 66—Set 205-1, PCB 71—Set 211-1 and Model 25TV2-43-9060A—Set 199-5) 9101, 9102A Tel. Rec. (See Model 15TV2-43-9101A—Set 152-4) 9169 (See Model 43-9169—Set 14-35) 9201 (See Model 43-9201—Set 24-14) 9230A (See Model 15RA37-43-9230A—Set 173-5) 9841A (See Model 94RA31-43-9841A—Set 79-3) 9855 (See Model RA37-43-9855—Set 227-5) 9856A (See Model 35RA4-43-9856A—Set 221-4) 98

CROSLY-Cont.

EU-177DLBU, TOLU (Ch. 396) Tel. Rec. (See PCB 73-Set 214-1 and Model EU-17COL-Set 193-3)
EU-177TDM (Ch. 380, 383) Tel. Rec. 186-3
EU-21CDB (Ch. 381, 384) Tel. Rec. 186-3
EU-21CDBU (Ch. 390 and UHF Ch. 391) Tel. Rec. (See PCB 80-Set 221-8 and Model EU-17COM-Set 186-3)
EU-21CDL (Ch. 387) (See PCB 73-Set 214-1 and Model EU-17COL-Set 193-3)
EU-21CDLBU, CDLU (Ch. 394) Tel. Rec. (See PCB 73-Set 214-1 and Model EU-17COL-Set 193-3)
EU-21EDM (Ch. 381, 384) Tel. Rec. 186-3
EU-21CDMU (Ch. 390 and UHF Ch. 391) Tel. Rec. (See PCB 80-Set 221-7 and Model EU-17COM-Set 186-3)
EU-21CDN (Ch. 381, 384) Tel. Rec. 186-3
EU-21CDNU (Ch. 390 and UHF Ch. 391) Tel. Rec. (See PCB 80-Set 221-1 and Model EU-17COM-Set 186-3)
EU-21COBA (Ch. 381, 384) Tel. Rec. 186-3
EU-21COBU (Ch. 390 and UHF Ch. 391) Tel. Rec. (See PCB 80-Set 221-1 and Model EU-17COM-Set 186-3)
EU-21COLB (Ch. 386) Tel. Rec. (Also see PCB 73-Set 214-1)
EU-21COLBU (Ch. 394) Tel. Rec. (See PCB 73-Set 214-1 and Model EU-17COL-Set 193-3)
EU-21COLBa (Ch. 387) Tel. Rec. (Also see PCB 73-Set 214-1)
EU-21COLBb (Ch. 386) Tel. Rec. (Also see PCB 73-Set 214-1)
EU-21COLC (Ch. 386) Tel. Rec. (Also see PCB 73-Set 214-1)
EU-21COLD (Ch. 387) Tel. Rec. (Also see PCB 73-Set 214-1)
EU-21COLU (Ch. 394) Tel. Rec. (See PCB 73-Set 214-1 and Model EU-17COL-Set 193-3)
EU-21COMa (Ch. 381, 384) Tel. Rec. 186-3
EU-21COMUa (Ch. 390 and UHF Ch. 391) Tel. Rec. (See PCB 80-Set 221-1 and Model EU-17COM-Set 186-3)
EU-21COS, COSB (Ch. 387) Tel. Rec. (See PCB 73-Set 214-1 and Model EU-17COL-Set 193-3)
EU-21COSBU, COSU (Ch. 394) Tel. Rec. (See PCB 73-Set 214-1 and Model EU-17COL-Set 193-3)
EU-21PDB, EU-21PDMU (Ch. 392, UHF Ch. 391 and Radio Ch. 362-1) Tel. Rec. (For TV Ch. only see PCB 73-Set 214-1 and Model EU-17COL-Set 193-3)
EU-21TOLB, TOLU (Ch. 393) Tel. Rec. (Also see PCB 73-Set 214-1)
E10EE, CT, RD, WE (Ch. 10E, 10E-1) 193-3
E15EE, CE, SL, TN, WE (Ch. 15-2CE) 201-3
E20CN, GY, MN, TN (Ch. 15-20E) 217-3
E30BE, GN, MN, TN (Ch. 30E, 30E-1) 206-3
E-75, CE, GN, RD, TN (Ch. 75E) 217-3
E-85, CE, GN, RD, TN (Ch. 85E) 217-3
E-9CBK, CE, GY, RD, WE (Ch. 90E) 217-4
F-17TOLB (Ch. 402) Tel. Rec. 223-5
F-17TOLU (Ch. 402-1) Tel. Rec. 223-5
F-17TOLH (Ch. 402) Tel. Rec. 223-5
F-17TOLU (Ch. 402-1) Tel. Rec. 223-5
F-21COLB (Ch. 404) Tel. Rec. 223-5
F-21COLBU (Ch. 404-1) Tel. Rec. 223-5
F-21CDLH (Ch. 404) Tel. Rec. 223-5
F-21CDLU (Ch. 404-1) Tel. Rec. 223-5
F-21COLU (Ch. 404-1) Tel. Rec. 223-5
F-21COLH (Ch. 404) Tel. Rec. 223-5
F-21COLB (Ch. 404-1) Tel. Rec. 223-5
F-21COLU (Ch. 404-1) Tel. Rec. 223-5
F-21TOLB (Ch. 403) Tel. Rec. 223-5
F-21TOLH (Ch. 403) Tel. Rec. 223-5
F-21TOLU (Ch. 403-1) Tel. Rec. 223-5
F-21TOLH (Ch. 403) Tel. Rec. 223-5
F-21TOLU (Ch. 403-1) Tel. Rec. 223-5
F-21CDLH, CDLU, CDHM, CDUM (Ch. 412-1) Tel. Rec. 234-5
F-21COLB, COLBH, COLH, COLU (Ch. 411, 411-1) Tel. Rec. 228-6
F-21COBU, COBU, COMH, COMU (Ch. 416, -1) Tel. Rec. 234-5
F-10BE, BK, CE, GN, RD (Ch. 10F) 218-4
G-17TOBH, G-17TOBK, G-17TOBU (Ch. 426) Tel. Rec. 249-5
G-17TOMH, G-17TOWEH, G-17TOWH, G-17TOWU (Ch. 426) Tel. Rec. 249-5

CROSLY-Cont.

S11-442MU, S11-444MU, S11-453MU (Ch. 331-4) Tel. Rec. 153-3
S11-459MU (Ch. 321-4) Tel. Rec. 153-3
S11-472BU, S11-474BU (Ch. 331-4) Tel. Rec. 153-3
S17COC1, S17COC2, S17COC3, S17COC4 (Ch. 331-4) Tel. Rec. 153-3
S17COC1, S17COC2, S17COC3 (Ch. 331-4) Tel. Rec. 153-3
9-101 58-8
9-102 50-4
9-103, 9-104W 60-10
9-105, 9-106W 59-7
9-113, 9-114W 53-9
9-117 51-5
9-118W 50-4
9-119, 9-120W 50-5
9-121, 9-122W 34-8
9-201, 9-202M, 9-203B 52-5
9-204, 9-205M 63-5
9-207M 57-6
9-209, 9-212M 53-10
9-213B (See Model 9-209-Set 53-10)
9-214M, 9-214ML 55-6
9-302 47-6
9-403M, 9-403M-2 Tel. Rec. 79-4
9-404M Tel. Rec. 79-4
9-407, 9-407M-1, 9-407M-2 Tel. Rec. 66-6
9-409M3 Tel. Rec. 94-3
9-413B, 9-413B-2, 9-414B Tel. Rec. 79-4
9-419M1, 9-419M1-LD, 9-419M2, 9-419M3, 9-419M3-LD Tel. Rec. 94-3
9-420M Tel. Rec. 79-4
9-422M, 9-422MA Tel. Rec. 81-6
9-423M Tel. Rec. 91A-4
9-424B Tel. Rec. 79-4
9-425 Tel. Rec. 95A-2
10-135, 10-136E, 10-137, 10-138, 10-139, 10-140 (Ch. 285) 93-3
10-307M, 10-308, 10-309 80-4
10-401 Tel. Rec. 95-2
10-404MU, 10-404MU Tel. Rec. 114-3
10-412MU Tel. Rec. 114-3
10-414MU Tel. Rec. 116-4
10-414M1 (Ch. 292) Tel. Rec. (See Model 10-414MU-Set 116-4)
10-416MU Tel. Rec. 116-4
10-416M1, 10-416M-U (Ch. 292) Tel. Rec. (See Model 10-414MU-Set 116-4)
10-418MU Tel. Rec. 114-3
10-419MU Tel. Rec. 104-6
10-420MU Tel. Rec. 114-3
10-421MU Tel. Rec. 106-4
10-427MU Tel. Rec. 125-1A
10-428MU Tel. Rec. 129-5
10-429M (Ch. 292) Tel. Rec. (See Model 10-414MU-Set 116-4)
10-429MU Tel. Rec. 116-4
11-100U, 11-101U, 11-102U, 11-103U, 11-104U, 11-105U (Ch. 301) 127-5
11-106U, 11-107U, 11-108U, 11-109U (Ch. 302) 155-5
11-114U, 11-115U, 11-116U, 11-117U, 11-118U, 11-119U (Ch. 300) 135-5
11-126U, 11-127U, 11-128U, 11-129U (Ch. 312) 123-5
11-207MU, 11-208BU (Ch. 325) 142-6
11-301U, 11-302U, 11-303U, 11-304U, 11-305U (Ch. 303) 124-3
11-441MU (Ch. 320) Tel. Rec. 126-4
11-442MU (Ch. 331) Tel. Rec. 126-4
11-443MU Tel. Rec. (See PCB 22-Set 126-4)
11-445MU (Ch. 321, -1, -2) Tel. Rec. 126-4
11-446MU (Ch. 325) Tel. Rec. 126-4
11-447MU (Ch. 321, -1, -2) Tel. Rec. 126-4
11-453MU (Ch. 331) Tel. Rec. 126-4
11-459MU, MU (Ch. 321, -1, -2) Tel. Rec. 126-4
11-460MU (Ch. 331) Tel. Rec. 126-4
11-461 WU (Ch. 320) Tel. Rec. 147-4
11-465WU (Ch. 321, -1, -2) Tel. Rec. 126-4
11-470BU (Ch. 331) Tel. Rec. 126-4
11-471 BU (Ch. 320) Tel. Rec. 147-4
11-4728BU (Ch. 331) Tel. Rec. 126-4
11-4738U Tel. Rec. (See PCB 22-Set 138-1 and Model 11-442-Set 126-4)
11-4755W (Ch. 321, -1, -2) Tel. Rec. 126-4
11-4768U (Ch. 325) Tel. Rec. 126-4
11-4778U (Ch. 321, -1, -2) Tel. Rec. 126-4
11-4838U (Ch. 331) Tel. Rec. 126-4
11-550MU (Ch. 337) 139-5
11-560BU (Ch. 337) 139-5
17COC1, 17COC2, 17COC3, 17COC4 (Ch. 331, -1, -2) Tel. Rec. (See Model 11-442-Set 126-4)
17COC1, 17COC2, 17COC3 (Ch. 331, -1) Tel. Rec. (See Model 11-442-Set 126-4)
46FA, 46FB 15-5
56FA, 56FB, 56FC 31-7
56PA, 56PB 10-9
56TA-L, 56TC-L 4-9
56TD 21-9
56TG 4-3
56TJ 5-14
56TN-L, 56TW-L 4-9

CROSLY-Cont.

56TP 8-5
56TZ 33-2
56TR, 56TS 17-11
56TJ (See Model 56TQ-Set 33-2)
56TQ (See Model 56TR-Set 38-2)
56TA 36-4
56TC (See Model 56TW-Set 38-2)
56TK 34-5
56TL 36-4
56TW 38-2
66CA, CP, CQ (See Model 66CS-Set 18-14)
66CS, 66CSM 18-14
66TA, 66TC, 66TW 5-15
66CP, 66CR 37-5
66TA, 66TW 40-4
66CR, 66CS 12-10
66CR, 66CS (Revised) 36-5
66TC 36-5
66CR (See Model 66TC-Set 36-5)
66TA, 66TC 38-3
66TA, 66TC (Revised) (See Set 43-8 and Model 66TA-Set 38-3)
106CP, 106CS 7-6
146CS 45-10
148CP, 148CQ 22-6
148CR (See Model 148CP-Set 42-6)
154927 Tel. UHF Conv. 211-5
Ch. 10E, 10E-1 (See Model E10BE)
Ch. 15-20E (See Model E15BE)
Ch. 30E, 30E-1 (See Model E30BE)
Ch. 75E (See Model E-75)
Ch. 85E (See Model E-85)
Ch. 90E (See Model E-90BK)
Ch. 110F (See Model F-110BE)
Ch. 292 Tel. Rec. (See Model 10-414MU)
Ch. 301 (See Model 11-100U)
Ch. 302 (See Model 11-106U)
Ch. 303 (See Model 11-301U)
Ch. 311, -1 (See Model D-25BE)
Ch. 312 (See Model 11-126U)
Ch. 320 (See Model 11-441MU)
Ch. 321, 321-1, 321-2 (See Model 11-445MU)
Ch. 321-4 Tel. Rec. (See Model S11-442MU)
Ch. 323 (See Model 11-443MU)
Ch. 323-3, 323-4 (See Model 20C01)
Ch. 323-6 (See Model 520C0C1)
Ch. 325 (See Model 11-446MU)
Ch. 330 (See Model 11-114U)
Ch. 331, -1, -2 (See Model 11-442)
Ch. 331-4 Tel. Rec. (See Model S11-442MU)
Ch. 333 (See Model 11-207MU)
Ch. 337 (See Model 11-550MU)
Ch. 356-1, 356-2 (See Model DU-17CDB)
Ch. 356-3, -4 (See Model DU-17CDB)
Ch. 357 Tel. Rec. (See Model DU-20CDM)
Ch. 357-1 (See Model DU-21CDM1)
Ch. 359 Tel. Rec. (See Model DU-17PDM)
Ch. 360, 361 Tel. Rec. (See Model DU-17PDB)
Ch. 380 (See Model EU-17CDM)
Ch. 381 (See Model EU-21CDB)
Ch. 383 (See Model EU-17COM)
Ch. 384 (See Model EU-21CDB)
Ch. 385, 386, 387 (See Model EU-17COL)
Ch. 386 (See Model EU-21COLBd)
Ch. 387 (See Model EU-21COLBe)
Ch. 390, 391 (See Model EU-21CDBU)
Ch. 392 (See Model EU-21PDBU)
Ch. 393 (See Model EU-21TOLBU)
Ch. 394 (See Model 21CDBLU)
Ch. 396 (See Model EU-17COLBU)
Ch. 402 (See Model F-17TOLB)
Ch. 402-1 (See Model F-17TOLBU)
Ch. 403 (See Model F-21TOLBH)
Ch. 403-1 (See Model F-21TOLBH)
Ch. 404 (See Model F-21CDBLU)
Ch. 404-1 (See Model F-21CDBLU)
Ch. 411, -1 (See Model F-24COLB)
Ch. 412, -1 (See Model F-24CDBH)
Ch. 416, -1 (See Model F-27CDBH)
Ch. 426 (See Model G-17TOBH)

CROYDON

C17FM Tel. Rec. (Also see PCB 57-Set 191-1) 186-4
C21FM, C21FTM (Also see PCB 57-Set 191-1) 186-4

CRYSTAL PRODUCTS (See Coronet)

DALBAR Barcombo Jr., Barcombo Sr. 10-14
WB "Tomatic" 8-34
100-1000 Series 10-15
400 9-9

DAVID BOGEN

"Twin" 213-3
AMB-1 TV Booster 246-3
AM901 195-6
BB-1A TV Booster 228-7
DB-10 (See Model DB10-Set 102-4)
DB20 237-6
DO10 231-5
DP-16 166-8
EQR 227-6
ET16 23-6
EX326 76-9
E66 85-4
E75 83-2
FC-1 250-6
FM801 198-4
FR-1 250-6
G-50 30-6
GO-50 26-9
GO-125 22-12
GX50 25-11
H15 80-6
H30 79-5
H50, H150, H2150 78-6
H623 71-8
HE-10 154-3

DAVID BOGEN-Cont.

H0H, H0L 80-5
H010 183-5
H050 84-5
H0125 10-13
HX30 82-4
HX50 75-7
HX-632 169-5
LOH, LOL 80-5
LP16 86-4
LSC 227-6
PHI0-1 (See Model PHI0-Set 68-5)
PP 242-5
PS-1 250-6
PX 183-5
PC10 68-5
PX15 72-8
RC 242-5
RP-1, RP-1L 241-5
RR500 243-3
RX 183-5
R300 238-7
R501 250-6
R602 67-8
R604 175-9
R701 227-6
UCT-1 UHF Conv. 249-6
UP16 86-4
2AR, 2RS 28-8
11D 5-7
11U 76-10
11X 74-2
21D 77-5
41D 76-10
21X 74-2

DEARBORN

100 22-13
DECCA DP11 24-15
DP20 19-3
PT-10 25-12

DELCO

R-705 42-7
R-1227, R-1228, R-1229 15-6
R-1230-A, R-1231-A, R-1232-A 14-33
R-1233 42-8
R-1234, R-1235 7-7
R-1236, R-1237 29-7
R-1238 38-4
R-1241 62-11
R-1242 31-8
R-1243 32-4
R-1244, R-1245, R-1246 52-6
R-1248, R-1249, R-1250 66-7
R-1251, R-1252 21-7
R-1253, R-1254, R-1255 47-7
R-1408, R-1409 9-11
R-177A Tel. Rec. 99A-3
TV-101 (See Model TV-102-Set 88-3)
TV-102 Tel. Rec. 88-3
TV-160 Tel. Rec. 85-5
TV-201 Tel. Rec. 59-8

DESOTO (See Mopar)

DETROLA

554-1-61A (See Aria Model 554-1-61A-Set 67-2)
558-1-49A 7-8
568-13-221D 9-10
571, 571A, 571B, 571L, 571AL, 571BL 10-16
571X, 571AX, 571BX 9-11
572-220-226A 8-6
577-1-6A 9-8
579 7-9
579-2-58B (See Model 579-Set 7-9)
582 19-14
610-A 55-8
611-A 50-6
626 Series 11-5
7156 48-6
7270 16-8

DEWALD

A500 4-22
A5001 (See Model A500-Set 4-22)
A500W (See Model A500-Set 4-22)
A501, A502, A503 4-22
A504, A505 16-9
A-509 26-10
A-509 31-9
A-514 27-6
A602, A605 16-10
A608 (See Model A602-Set 16-10)
B-400 35-3
B-401 34-6
B-402 45-8
B-403 52-7
B-504 43-9
B-506 38-5
B-510 34-7
B-512 35-4
B-515 63-6
B-612 42-9
B-614 56-9
BT-100, BT-101 Tel. Rec. 79-6
C-516 64-4
C-800 69-7
CT-101 Tel. Rec. 79-6
CT-102, CT-103, CT-104 Tel. Rec. 82-5
D-E517A 167-5
D-508 16-5
D-510 131-4
D-518 100-5
D519 (See Model B-506-Set 38-5)
D-616 102-5
DT-120, DT-122 Tel. Rec. 100-6
DT-161 Tel. Rec. 82-5
DT-162, DT-163 Tel. Rec. 118-5
DT-162R, DT-163A, R Tel. Rec. (Also see PCB 58-Set 192-1) 136-7
D-190 Tel. Rec. 118-5
D-190D Tel. Rec. (Also see PCB 58-Set 192-1) 136-7
DT-1020, DT-1020A Tel. Rec. 100-6

DEWALD-Cont.

DT-1030, DT-1030A Tel. Rec. 100-6
DT-X-160 Tel. Rec. 100-6
E-520 128-5
E-522 141-5
ET-140, ET-141 Tel. Rec. 118-5
HX-632 169-5
ET-140R, ET-141R Tel. Rec. (Also see PCB 58-Set 192-1) 136-7
E-170, ET-171 Tel. Rec. (Also see PCB 58-Set 192-1) 136-7
ET-171-20 Tel. Rec. 208-3
ET-172 Tel. Rec. (Also see PCB 58-Set 192-1) 136-7
ET-190D, R Tel. Rec. (Also see PCB 58-Set 192-1) 136-7
ET-190D (Revised) Tel. Rec. 208-3
ET-200 Tel. Rec. (See PCB 58-Set 192-1 and Model DT-162R-Set 136-7)
FT-200 (Revised) Tel. Rec. 208-3
FT-201 Tel. Rec. (See PCB 58-Set 192-1 and Model DT-162R-Set 136-7)
F-404 181-5
F-405 198-5
F-523 170-5
G-174 Tel. Rec. 208-3
G-201 Tel. Rec. 208-3
G-210, G-211 Tel. Rec. 208-3
G-220 220-3
H-300 UHF Conv. 250-7
H-527 239-5
H-528 234-7
H-533 248-4
H111 71-9

DODGE (See Mopar)

DORN'S (See Bell Air)

DOUGLAS

327 (Ch. S-103, T-103) Tel. Rec. 246-4

DREXEL (Mutual Buying Syndicate)

17CG1, 17TW Tel. Rec. (Similar to Chassis) 149-13

DUKANE

1A45-A 184-5
1A300, 1B300 189-6
1032 220-3
4A100 186-5
4B100 (See Model 4A100-Set 186-5)
4C25 Flexiphone 187-4
4C100 200-4

DUMONT

RA-103 Tel. Rec. (Also see PCB 6-Set 108-1) 90-3
RA-103D Tel. Rec. (Also see PCB 9-Set 114-1) 93-4
RA-104 Tel. Rec. (Also see PCB 9-Set 114-1) 93-4
RA-104A Tel. Rec. (Also see PCB 6-Set 108-1) 93-3
RA-106 Tel. Rec. (Supp. to RA-105, Set 72) (Also see PCB 6-Set 108-1) 99A-4
RA-108A Tel. Rec. 95-3
RA-109A-FAS Tel. Rec. (See PCB 54-Set 188-1 and Model RA-109-Set 110-7)
RA-109-A1, -A2, -A3, -A5, -A6, -A7 Tel. Rec. (Also see PCB 14-Set 124-1) 110-7
RA-110A Tel. Rec. (Also see PCB 9-Set 114-1) 93-4
RA-111-A1, -A2, -A4, -A5 Tel. Rec. 106-6
RA-112-A1, -A2, -A3, -A4, -A5, -A6 Tel. Rec. (Also see PCB 38-Set 170-1) 119-5
RA-117-A1, -A3, -A5, -A6, -A7 Tel. Rec. 131-5
RA-119A Tel. Rec. 156-5
RA-120 Tel. Rec. (See PCB 51-Set 185-1 and Model RA-113-Set 119-5)
RA-130A Tel. Rec. (See PCB 54-Set 188-1 and Model RA-109-Set 110-7)
RA-147A Tel. Rec. (See PCB 49-Set 183-1 and Model RA-117A-Set 131-5)
RA-160, -A1 Tel. Rec. (Also see PCB 55-Set 189-1) 179-4
RA-162, -B1, -B4, -B5, -B6, -B7, -B21 through 26 Tel. Rec. (Also see PCB 55-Set 189-1) 179-4
RA-164, -A1 Tel. Rec. (Also see PCB 60-Set 194-1 and PCB 69-Set 206-1) 189-7
RA-165, -B1, -B2, -B3, -B6, -B7, -B21 through -B26 Tel. Rec. (Also see PCB 60-Set 194-1 and PCB 69-Set 206-1) 189-7
RA-166, RA-167, RA-168, RA-169, RA-170, RA-171 Tel. Rec. 216-2
RA-306, RA-307 Tel. Rec. 216-2
C-800 69-7
Andover Model RA-117-A6 (See Model RA-117A)
Andover Model RA-147A (See Model RA-147A)
Ardmore Model RA-112-A1, -A4 (See Model RA-112A)
Banbury Model RA-162-B4 (See Model RA-162)
Beverly Model RA-165-B2 (See Model RA-165)
Bradford (See Model RA-108A)
Bradford Models RA-306, RA-307 (See Model RA-306)
Bristol Models RA-306, RA-307 (See Model RA-306)
Brookville Model RA-113-B1, -B2 (See Model RA-113)
Burlingame Model RA-113-B5, -B6 (See Model RA-113)

DUMONT-EMERSON

DUMONT-Cont.

Canterbury Model RA-103 (See Model RA-103)	19-16
Carlton Model RA-117-A3 (See Model RA-117A)	19-16
Charham (See Model RA-103)	
Chatham Model RA-166 (See Model RA-166)	27-7
Chatham Model RA-168, RA-169 (See Model RA-168)	36-3
Chester (See Model RA-147A)	
Clinton Model RA-164-A1 (See Model RA-164)	1-25
Club 20 (See Model RA-106A)	102-7
Colony (See Model RA-105A)	104
Devon Model RA-160-A1 (See Model RA-160)	103-14
Dynasty (See Model RA-162)	105
Essex Model RA-167 (See Model RA-167)	106
Fairfield (See Model RA-110A)	108
Flanders Model RA-162-B5 (See Model RA-162)	121
Guilford Model RA-111-A2, -A5 (See Model RA-111A)	131
Hampton Models RA-306, RA-307 (See Model RA-306)	104
Hanover Model RA-109-A2, -A6 (See Model RA-109A)	105
Hanover (See Model RA-109A-FAS)	106
Hanover Model RA-162 (See Model RA-162)	108
Hanover II Model RA-170 (See Model RA-170)	121
Hanover II Model RA-171 (See Model RA-171)	131
Harford Models RA-306, RA-307 (See Model RA-306)	104
Hastings (See Model RA-104A)	105
Lynwood Model RA-167 (See Model RA-167)	106
Lynwood Model RA-169 (See Model RA-169)	108
Manchu (See Model RA-106A)	121
Mansfield (See Model RA-108A)	131
Meadowbrook Model RA-103 (See Model RA-103)	104
Meadowbrook II (See Model RA-147A)	105
Millard Model RA-165-B1 (See Model RA-165)	106
Mt. Vernon Model RA-112-A3, -A6 (See Model RA-112A)	108
Newbury (See Model RA-162)	121
Newbury II Model RA-170 (See Model RA-170)	131
Newbury II Model RA-171 (See Model RA-171)	104
Newport Models RA-306, RA-307 (See Model RA-306)	105
Oxford Model RA-167 (See Model RA-167)	106
Park Lane Model RA-117-A7 (See Model RA-117A)	108
Parklane (See Model RA-147A)	121
Putman Model RA-111-A1, -A4 Tel. Rec. (See Model RA-111A)	131
Revere Model RA-113-B3, -B4 (See Model RA-113)	104
Ridgewood Model RA-165-B4 (See Model RA-165)	105
Ridgewood "41" Model RA-167 (See Model RA-167)	106
Royal Sovereign (See Model RA-119A)	108
Rumton (See Model RA-103D)	121
Rutland Models RA-306, RA-307 (See Model RA-306)	131
Savoy (See Model RA-103)	104
Sheffield (See Model RA-103D)	105
Sheffield Models RA-306, RA-307 (See Model RA-306)	106
Shelburne Model RA-165-B5 (See Model RA-165)	108
Sherbrooke Models RA-109-A3, -A7 (See Model RA-109A)	109
Sherbrooke (See Model RA-109A-FAS)	110
Sherbrooke (See Model RA-130A)	111
Someriset (See Model RA-162)	112
Someriset II Model RA-170 (See Model RA-170)	113
Someriset II Model RA-171 (See Model RA-171)	114
Stratford (See Model RA-105A)	115
Strathmore Model RA-117-A5 (See Model RA-117A)	116
Sumter Model RA-117-A1 (See Model RA-117A)	117
Suxest (See Model RA-105B)	118
Sutton Model RA-103 (See Model RA-103)	119
Tarrytown Models RA-113-B7, -B8 (See Model RA-113)	120
Tarrytown (See Model RA-120)	121
Wakefield Model RA-165-B3 (See Model RA-164)	122
Wakefield "41" Model RA-167 (See Model RA-167)	123
Warren Models RA-306, RA-307 (See Model RA-306)	124
Warwick Models RA-306, RA-307 (See Model RA-306)	125
Wellington (See Model RA-104A)	126
Westbrook Models RA-306, RA-307 (See Model RA-306)	127
Westbury (See Model RA-105A)	128
Westbury II (See Model RA-109A-FAS)	129
Westerly Model RA-112-A2, -A5 (See Model RA-112A)	130
Westwood (See Model RA-110A)	131
Whitehall (See Model RA-105A)	132
Whitehall II (See Model RA-130A)	133
Whitehall II Model RA-162-B7 (See Model RA-162)	134
Wickford Model RA-162-B1 (See Model RA-162)	135
Wimbledon Model RA-162-B6 (See Model RA-162)	136
Windsor Models RA-306, RA-307 (See Model RA-306)	137
Winslow (See Model RA-109A-FAS)	138
Winslow Model RA-109-A1, -A5 (See Model RA-109A)	139
Winthrop Model RA-103 (See Model RA-103)	140

DUOSONIC

K1, K2	19-15	
K3, K4	19-16	
DYNAVOX		
AP-514 (Ch. AT.)	28-9	
M-510	15-8	
Swingmaster	27-7	
3-P-801	36-3	
ECA		
101 (Ch. AA)	1-25	
102	14-7	
104	13-14	
105	16-11	
106	7-10	
108	3-6	
121	13-15	
131	16-12	
132	45-9	
201	15-9	
204	32-5	
ECHOPHONE (Also see Hallicrafters)		
EC-113	3-13	
EC-306	14-8	
EC-403, EC-404	22-14	
TC-600	4-18	
EX-102, EX-103	64-5	
EX-306 (See Model EC-306)	14-8	
EDWARDS		
Fidelotuner	33-4	
ECOR (Also see Recorder Listing)		
15	135-6	
EKOTAPE (See Recorder Listing)		
ELCAR		
602	5-19	
ELECTONE		
TST53	12-34	
ELECTRO		
B20	14-9	
ELECTROMATIC		
APH301-A, APH301-C	7-11	
606A, 607A	5-32	
ELECTRO-TONE		
555	13-17	
706, 712 (See Model 555)	13-16	
ELECTRO-VHF 3300 Tel. Conv.		222-5
ELECTRONIC CORP. OF AMERICA (See ECA)		
ELECTRONIC SPECIALTY CO. (See Rangex)		
E/L (ELECTRONIC LABS.)		
75 (Sub-Station)	20-6	
78E, K, M, W (See Model 2701)	27-11	
76RU ("Radio-Utiliphone")	20-6	
710B, 710M, 710T, 710W, Orthosonic (Ch. 2875)	20-7	
710PB, 710PC Orthosonic (Ch. 2887)	24-16	
2660 "Master Utiliphone"	8-9	
2701	4-28	
3000 Orthosonic	31-10	
EMERSON		
501, 502 (Ch. 120000, 120029)	2-1	
503 (Ch. 120000, 120029)	1-18	
504 (Ch. 120000, 120029)	2-1	
505 (Ch. 120002)	8-9	
505 (Ch. 120041) (See Model 523 Set 5-27)	10-1	
506	6-9	
507	8-10	
508 (Ch. 120008)	7-12	
509	8-10	
510, 510A (Ch. 120000, 120029)	5-36	
511	8-10	
511 (Ch. 120010) (See Model 541 Set 16-23)	8-10	
512 (Ch. 120006)	9-12	
512 (Ch. 120056)	26-11	
514 (Ch. 120007)	27-8	
515, 515 Res.	12-11	
515, 516 (Ch. 120056)	26-11	
517 (Ch. 120010) (See Model 541 Set 16-13)	8-10	
518	8-10	
519 (Ch. 120030)	30-7	
520 (Ch. 120000, 120029)	2-17	
521 (Ch. 120013, 120031)	7-13	
522	8-10	
523	5-37	
524	17-12	
525	20-8	
521-B (Ch. 120038)	21-13	
529, 529-9 (Ch. 120028)	18-15	
530 (Ch. 120006, Ch. 120056)	32-6	
531, 532, 533	11-6	
534 (Ch. 120007)	27-8	
535	20-9	
536 (Ch. 120036)	21-14	
536A	24-17	
537	23-7	
538 (Ch. 120051) (See Model 549 Set 26-12)	9-13	
539	9-13	
540A (Ch. 120042)	20-10	
541	16-13	
542 (See Model 521 Set 7-13)	16-13	
543, 544 (Ch. 120046)	19-30	
545 (Ch. 120047) Tel. Rec. Photo-fact Servicer	82	
546 (Ch. 120049)	21-15	
547A (Ch. 120050)	25-13	
548 (Ch. 120051)	30-8	
549 (Ch. 120051)	26-12	
550 (Ch. 120060) (See Model 512 Set 9-12)	26-12	

EMERSON-Cont.

550 (Ch. 120056)	26-11
551A	24-17
552	20-8
553A	24-17
556, 557 (Ch. 120018B)	70-4
557B (Ch. 120088)	43-10
558 (Ch. 120058)	31-11
559A (Ch. 120059)	31-12
560 (Ch. 120016)	25-14
561 (Ch. 120018)	63-7
563 (Ch. 120063B)	73-4
564 (Ch. 120027) (See Model 540A Set 20-10)	73-4
565 (Ch. 120018B)	70-4
566 (Ch. 120051) (See Model 549 Set 26-12)	70-4
567 (Ch. 120016) (See Model 560 Set 25-14)	70-4
567 (Ch. 120042) (See Model 540A Set 20-10)	70-4
568A (Ch. 120070A)	58-9
569A (Ch. 120062A)	42-10
570 (Ch. 120064)	97-3
571 (Ch. 120066) Tel. Rec.	46-25
571 (Ch. 120086B) Tel. Rec.	76-11
572 (Ch. 120065) (See Model 540A Set 20-10)	76-11
573B (Ch. 120039B)	42-11
574 (Ch. 120064)	97-3
575 (Ch. 120068A, 120068B)	85-6
576A (Ch. 120069A)	40-5
577B (Ch. 120012B)	41-6
578 (Ch. 120050) (See Model 547A Set 25-13)	41-6
579A (Ch. 120034A)	61-6
580 (Ch. 120064)	97-3
581 (Ch. 120014A, B)	68-7
582 (See Model 548 Set 30-8)	68-7
583 (See Model 573B Set 42-11)	68-7
584 (See Model 558 Set 31-11)	68-7
585 (Ch. 120025B) Tel. Rec.	61-7
586 (Ch. 120023B, 120083B)	72-9
587 (Ch. 120033A, B)	71-10
588 (See Model 547A Set 25-13)	71-10
590 (Ch. 120101A, B)	87-5
591 (Ch. 120055A)	67-9
593 (Ch. 120063B)	73-4
594, 595 (Ch. 120071A)	68-7
596	61-6
597 (Ch. 120073B)	90-5
599 (Ch. 120075B)	69-8
600 (Ch. 120101B) Tel. Rec. (Also see PCB 9 Set 114-1)	87-6
601 (Ch. 120075B)	69-8
602 (Ch. 120072A, 120082A)	56-10
603 (Ch. 120063B)	73-4
604A (See Model 576A Set 40-5)	66-8
605 (Ch. 120076B)	66-8
606 (Ch. 120066) Tel. Rec.	46-25
606 (Ch. 120066B) Tel. Rec.	46-25
606 (Ch. 120086B-D) Tel. Rec.	76-11
606 (Ch. 120086B) Tel. Rec.	76-11
607 (Ch. 120074A)	90-5
608A (Ch. 120098B) Tel. Rec.	84-6
609 (Ch. 120084-B) Tel. Rec.	90-6
610 (Ch. 120100A, B)	71-10
611, 612 (Ch. 120087B-D) Tel. Rec.	76-11
613A (Ch. 120085A, B)	79-7
614, B, BC, C (Ch. 120110, B, BC, C) Tel. Rec.	97-4
614D (Ch. 120095-B) Tel. Rec.	97-4
615 (Ch. 120018B)	95A-3
616 (Ch. 120100A, B)	71-10
619 (Ch. 120092D) Tel. Rec.	76-11
620 (Ch. 120091D-QD) Tel. Rec.	76-11
EMERSON	
621 (Ch. 120098B) Tel. Rec.	108-5
622 (Ch. 120098P) Tel. Rec.	108-5
623 (Ch. 120101A, B)	87-5
624 (Ch. 120087B-D) Tel. Rec.	76-11
625 (Ch. 120105B)	103-8
626 (Ch. 120104B, 120104B1) Tel. Rec.	84-6
627 (Ch. 120107B) Tel. Rec.	76-11
628 (Ch. 120098B) Tel. Rec.	108-5
629 (Ch. 120114B) Tel. Rec. (See Model 631 Set 93A-6)	108-5
629B, 629C (Ch. 120120) Tel. Rec.	119-6
629D (Ch. 120124B) Tel. Rec.	116-5
630 (Ch. 120099B) Tel. Rec.	108-5
631 (Ch. 120109) Tel. Rec.	93A-6
632 (Ch. 120096B) Tel. Rec.	93A-6
633 (Ch. 120114) Tel. Rec.	93A-6
634B (Ch. 120097B)	114-4
635 (Ch. 120108)	92-1
636A (Ch. 120106A)	99-7
637, B, BC, C (Ch. 120110, B, BC, C) Tel. Rec.	97-4
637A (Ch. 120095-B) Tel. Rec.	97-4
638 (Ch. 120087D) Tel. Rec. (See Model 571 Set 76-11)	95A-3
639 (Ch. 120103B) Tel. Rec. (Also see PCB 9 Set 114-1)	87-6
640 (Ch. 120112)	93-5
641B (Ch. 120125B)	98-3
642 (Ch. 120117A)	98-3
643A (Ch. 120111A)	91-4
644, B, BC, C (Ch. 120113, B, BC, C) Tel. Rec.	97-4
645 (Ch. 120115)	94-4
646A (Ch. 120121A)	102-6
646B (Ch. 120121B)	102-6
647, B, BC, C (Ch. 120113, B, BC, C) Tel. Rec.	97-4
648B (Ch. 120110E) Tel. Rec.	97-4
648B (Ch. 120134B, G, H) Tel. Rec. (Also see PCB 48 Set 182-1 and Model 661B Set 137-4)	106-7
649A (Ch. 120094A) Tel. Rec.	106-7
650 (Ch. 120113C) Tel. Rec. (See Model 614 Set 97-4)	113-2
650 (Ch. 120118B) Tel. Rec.	113-2

EMERSON-Cont.

650B (Ch. 120118B) Tel. Rec. (See Model 650 Set 113-2)	113-2
650D (Ch. 120123-B) Tel. Rec. (Also see PCB 48 Set 182-1)	109-3
650F (Ch. 120138-B) Tel. Rec.	133-1A
6518 (Ch. 120120) Tel. Rec.	119-6
651C (Ch. 120109) Tel. Rec.	93A-6
651C (Ch. 120124) Tel. Rec.	116-5
651D (Ch. 120124, B) Tel. Rec.	116-5
652 (Ch. 120032B)	98-3
653 (Ch. 120080B)	98-3
653B (Ch. 120136-B)	159-5
654 (Ch. 120118B) Tel. Rec.	113-2
654B (Ch. 120118B) Tel. Rec. (See Model 654 Set 113-2)	113-2
654D (Ch. 120123B) Tel. Rec. (Also see PCB 48 Set 182-1)	109-3
654F (Ch. 120138-B) Tel. Rec.	133-1A
655B (Ch. 120123-B) Tel. Rec.	109-3
655D (Ch. 120123B) Tel. Rec. (See Model 650D Set 109-3)	133-1A
655F (Ch. 120138-B) Tel. Rec.	133-1A
656B, 657B (Ch. 120122B)	111-5
658B (Ch. 120124, B) Tel. Rec.	116-5
658C (Ch. 120124) Tel. Rec. (See Model 629D Set 116-5)	116-5
660B (Ch. 120133B) Tel. Rec.	131-6
661B (Ch. 120134B, G, H) Tel. Rec. (Also see PCB 48 Set 182-1)	137-4
662B (Ch. 120127-B) Tel. Rec. (Also see PCB 18 Set 130-1)	125-6
663B (Ch. 120128-B) Tel. Rec. (Also see PCB 18 Set 130-1)	125-6
664B (Ch. 120133-B) Tel. Rec.	131-6
665-B (Ch. 120131-B and Radio Ch. 120130-B) Tel. Rec.	146-6
666B (Ch. 120135B, G, H and Radio Ch. 120132B) Tel. Rec. (Also see PCB 27 Set 148-1)	131-6
667B, 668B (Ch. 120134B, G, H) Tel. Rec. (Also see PCB 48 Set 182-1)	137-4
669B (Ch. 120129B, D) Tel. Rec. (Also see PCB 24 Set 142-1 and PCB 47 Set 181-1)	126-5
671B (Ch. 120137-B)	118-6
671D (Ch. 120137D) (See Model 671B Set 118-6)	131-7
672B (Ch. 120097B)	131-7
673B (Ch. 120133-B) Tel. Rec.	131-6
674B (Ch. 120134B, G, H) Tel. Rec. (Also see PCB 48 Set 182-1)	137-4
675B (Ch. 120129B, D) Tel. Rec. (Also see PCB 24 Set 142-1 and PCB 47 Set 181-1)	126-5
676B (Ch. 120140B) Tel. Rec.	128-6
676D (Ch. 120144B, G, H) Tel. Rec. (Also see PCB 48 Set 182-1)	138-4
676F (Ch. 120143B) Tel. Rec. (Also see PCB 50 Set 184-1)	148-6
677B, 678B (Ch. 120134B, G, H) Tel. Rec. (Also see PCB 48 Set 182-1)	137-4
679B (Ch. 130116-B)	142-7
680B (Ch. 120144-B, G, H) Tel. Rec. (Also see PCB 48 Set 182-1)	138-4
680D (Ch. 120140B) Tel. Rec.	128-6
680D (Ch. 120144B, G, H) Tel. Rec. (Also see PCB 48 Set 182-1 and Model 676D Set 138-4)	138-4
681B (Ch. 120140B) Tel. Rec.	128-6
681D (Ch. 120144B, G, H) Tel. Rec. (Also see PCB 48 Set 182-1)	138-4
681F (Ch. 120143B, H) Tel. Rec. (Also see PCB 50 Set 184-1)	148-6
684B, 685B (Ch. 120134B, G, H) Tel. Rec.	137-4
686B (Ch. 120144B, G, H) Tel. Rec. (Also see PCB 48 Set 182-1)	138-4
6	

EMERSON-Cont.

753D [Ch. 120180-D] Tel. Rec. 243-4
753E [Ch. 120180-D] Tel. Rec. 243-4
753F [Ch. 120198-D] Tel. Rec. 243-4
754D [Ch. 120176-B] (See Model 745E-Set 227-7)
755A, B [Ch. 120174-B] Tel. Rec. 243-4
756B [Ch. 120125-B] (See Model 641E-Set 120-5)
757D [Ch. 120182-D] Tel. Rec. (Also See PCB 103-Set 249-1) 235-5
757F [Ch. 120194-D] Tel. Rec. (See PCB 51-Set 195-1, PCB 71-Set 211-1, PCB 86-Set 229-1 and Model 716D-Set 190-2)
757J [Ch. 120168-D] Tel. Rec. (See PCB 61-Set 195-1, PCB 71-Set 211-1, PCB 86-Set 229-1 and Model 716D-Set 190-2)
758F [Ch. 120182-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
759C [Ch. 120195-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 785K-Set 235-5)
760D [Ch. 120191-D] Tel. Rec. 243-4
760F [Ch. 120194-D] Tel. Rec. (See PCB 51-Set 195-1, PCB 71-Set 211-1, PCB 86-Set 229-1 and Model 716D-Set 190-2)
761C [Ch. 120180-D] Tel. Rec. 243-4
762D [Ch. 120191-D] Tel. Rec. 243-4
762F [Ch. 120190-D] Tel. Rec. 243-4
764F [Ch. 120166-D] Tel. Rec. (See PCB 65-Set 202-1, PCB 86-Set 218-1 and Model 721D-Set 197-5)
765D [Ch. 120173-D] Tel. Rec. (See Model 740D)
766D [Ch. 120210-D] Tel. Rec. 243-4
767A, B [Ch. 120192-B] Tel. Rec. 243-4
767C [Ch. 120169-B] Tel. Rec. (See Model 711F-Set 206-4)
768A [Ch. 120193-D] Tel. Rec. 243-4
768C [Ch. 120174-B] Tel. Rec. (See Model 752A-Set 243-4)
769F [Ch. 120173-D] Tel. Rec. (See Model 740D)
770C [Ch. 120205-D] Tel. Rec. 243-4
771A, B [Ch. 120192-B] Tel. Rec. 243-4
771C [Ch. 120169-B] Tel. Rec. (See Model 711F-Set 206-4)
771D [Ch. 120192-D] Tel. Rec. 243-4
772A [Ch. 120193-B] Tel. Rec. 243-4
773A [Ch. 120192-B] Tel. Rec. 243-4
774A [Ch. 120193-B] Tel. Rec. 243-4
775A, B [Ch. 120192-F and Radio Ch. 120183-F] 243-4
776A [Ch. 120193-F and Radio Ch. 120184-B] Tel. Rec. (See Model 775A-Set 243-4)
778B [Ch. 120199B] 248-6
779B [Ch. 120170-B] 251-6
780A [Ch. 120171-B] Tel. Rec. (See Model 736B)
781A, B [Ch. 120196-B] Tel. Rec. (Also See PCB 103-Set 249-1) 235-5
781E [Ch. 120206-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
782D [Ch. 120166-D] Tel. Rec. (See Model 721D)
784A [Ch. 120174-B] Tel. Rec. 243-4
784E [Ch. 120197-B] Tel. Rec. (Also See PCB 103-Set 249-1) 235-5
784G [Ch. 120197-D] Tel. Rec. (Also See PCB 103-Set 249-1) 235-5
784K [Ch. 120197-B] Tel. Rec. (See PCB 103-Set 249-1 and Model 784E-Set 235-5)
784M [Ch. 120211-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
785C, E [Ch. 120198-B] Tel. Rec. 243-4
785K [Ch. 120195-D] Tel. Rec. (Also See PCB 103-Set 249-1) 235-5
788B [Ch. 120201B] 250-8
791D [Ch. 120210-D] Tel. Rec. 243-4
792D [Ch. 120206-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
793E [Ch. 120211-F] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
794A [Ch. 120193-B] Tel. Rec. (See Model 768A-Set 243-4)
795C [Ch. 120192-B] Tel. Rec. 243-4
799E [Ch. 120209-F] Tel. Rec. 243-4
801 [Ch. 120154-B] (See Model 70-Set 184-6)
1000C [Ch. 120206-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1001F [Ch. 120208-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1002 [Ch. 120206-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1003 [See Model 1002-Set 16-14]
1003E [Ch. 120208-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1003G [Ch. 120211-F] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1004C [Ch. 120206-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1005E [Ch. 120208-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1006C [Ch. 120206-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1007E [Ch. 120208-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1008E [Ch. 120206-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1009C [Ch. 120208-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1010C [Ch. 120206-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1011C [Ch. 120208-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1012D [Ch. 120182-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1013C [Ch. 120195-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 785K-Set 235-5)
Ch. 120028B (See Model 585)
Ch. 120047 (See Model 545)
Ch. 120066 (See Model 571)
Ch. 120068B (See Model 571)
Ch. 120084B (See Model 609)
Ch. 120086B (See Model 571)
Ch. 120087B-D (See Model 611)
Ch. 120088B (See Model 585)
Ch. 120089B (See Model 608A)
Ch. 120091D-QD (See Model 620)
Ch. 120092D (See Model 619)
Ch. 120094A (See Model 645A)
Ch. 120095-B (See Model 614D)
Ch. 120096B (See Model 632)
Ch. 120098B (See Model 621)
Ch. 120098P (See Model 622)
Ch. 120099B (See Model 600)
Ch. 120103B (See Model 630)
Ch. 120104B, BJ (See Model 626)
Ch. 120107B (See Model 627A)
Ch. 120109 (See Model 631)
Ch. 120111-D, B, BC, C (See Model 614, B, BC, C)
Ch. 120110E (See Model 644B)
Ch. 120113, B, BC, C (See Model 644, B, BC, C)
Ch. 120114 (See Model 633)
Ch. 120115 (See Model 629)
Ch. 120118B (See Model 650)
Ch. 120120 (See Model 629B, C)
Ch. 120123B (See Model 650D)
Ch. 120124 (See Model 651C)
Ch. 120124B (See Model 629D)
Ch. 120127-B (See Model 628B)
Ch. 120128-B (See Model 643B)
Ch. 120129-B (See Model 669B)
Ch. 120131-B (See Model 665B)
Ch. 120133B (See Model 660B)
Ch. 120134B, G, H (See Model 661B)
Ch. 120135B, G, H (See Model 666B)
Ch. 120136-B (See Model 663B)
Ch. 120138-B (See Model 650F)
Ch. 120140B (See Model 676B)
Ch. 120142B (See Model 686A)
Ch. 120143B, H (See Model 676F)
Ch. 120144B, G, H (See Model 676D)
Ch. 120149A (See Model 725A)
Ch. 120150-B (See Model 718B)
Ch. 120151 (See Model 734B)
Ch. 120152-B (See Model 731D)
Ch. 120152-F (See Model 733F)
Ch. 120153-B (See Model 700B)
Ch. 120154-B (See Model 794)
Ch. 120155A, B (See Model 705A, B)
Ch. 120158-B (See Model 740D)
Ch. 120160-B (See Model 699D)
Ch. 120162-A (See Model 709A)
Ch. 120163-D (See Model 716D)
Ch. 120164-B (See Model 718B)
Ch. 120165-D (See Model 735A)
Ch. 120167-D (See Model 731D)
Ch. 120168-D (See Model 716F)
Ch. 120169-B (See Model 711F)
Ch. 120169-D (See Model 720F)
Ch. 120169F (See Model 736F)
Ch. 120170-B (See Model 729B)
Ch. 120171-B (See Model 736B)
Ch. 120172A, B (See Model 737A, B)
Ch. 120173-D (See Model 740D)
Ch. 120174-B (See Model 752A)
Ch. 120175-B (See Model 748B)
Ch. 120176-B (See Model 745B)
Ch. 120177-B (See Model 746B)
Ch. 120178 (See Model 747)
Ch. 120180-D (See Model 753D)
Ch. 120182-D (See Model 741F)
Ch. 120184-B (See Model 755A)
Ch. 120185-B (See Model 712G)
Ch. 120190-D (See Model 760H)
Ch. 120191-D (See Model 760D)
Ch. 120192-B (See Model 787A)
Ch. 120192-D (See Model 771D)
Ch. 120192-F (See Model 775A)
Ch. 120193-B (See Model 758A)
Ch. 120193-F (See Model 726A)
Ch. 120194-D (See Model 757F)
Ch. 120195-D (See Model 785K)
Ch. 120198-B (See Model 731A)
Ch. 120197-F (See Model 784E)
Ch. 120197-D (See Model 784G)
Ch. 120198-D (See Model 753F)
Ch. 120199-B (See Model 778B)
Ch. 120201-B (See Model 738B)
Ch. 120206-D (See Model 781E)
Ch. 120208-D (See Model 1001E)
Ch. 120209-D (See Model 770C)
Ch. 120209-F (See Model 799E)

EMERSON-Cont.

1003 [See Model 1002-Set 16-14]
1003E [Ch. 120208-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1003G [Ch. 120211-F] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1004C [Ch. 120206-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1005E [Ch. 120208-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1006C [Ch. 120206-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1007E [Ch. 120208-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1008E [Ch. 120206-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1009C [Ch. 120208-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1010C [Ch. 120206-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1011C [Ch. 120208-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1012D [Ch. 120182-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 741F-Set 235-5)
1013C [Ch. 120195-D] Tel. Rec. (See PCB 103-Set 249-1 and Model 785K-Set 235-5)
Ch. 120028B (See Model 585)
Ch. 120047 (See Model 545)
Ch. 120066 (See Model 571)
Ch. 120068B (See Model 571)
Ch. 120084B (See Model 609)
Ch. 120086B (See Model 571)
Ch. 120087B-D (See Model 611)
Ch. 120088B (See Model 585)
Ch. 120089B (See Model 608A)
Ch. 120091D-QD (See Model 620)
Ch. 120092D (See Model 619)
Ch. 120094A (See Model 645A)
Ch. 120095-B (See Model 614D)
Ch. 120096B (See Model 632)
Ch. 120098B (See Model 621)
Ch. 120098P (See Model 622)
Ch. 120099B (See Model 600)
Ch. 120103B (See Model 630)
Ch. 120104B, BJ (See Model 626)
Ch. 120107B (See Model 627A)
Ch. 120109 (See Model 631)
Ch. 120111-D, B, BC, C (See Model 614, B, BC, C)
Ch. 120110E (See Model 644B)
Ch. 120113, B, BC, C (See Model 644, B, BC, C)
Ch. 120114 (See Model 633)
Ch. 120115 (See Model 629)
Ch. 120118B (See Model 650)
Ch. 120120 (See Model 629B, C)
Ch. 120123B (See Model 650D)
Ch. 120124 (See Model 651C)
Ch. 120124B (See Model 629D)
Ch. 120127-B (See Model 628B)
Ch. 120128-B (See Model 643B)
Ch. 120129-B (See Model 669B)
Ch. 120131-B (See Model 665B)
Ch. 120133B (See Model 660B)
Ch. 120134B, G, H (See Model 661B)
Ch. 120135B, G, H (See Model 666B)
Ch. 120136-B (See Model 663B)
Ch. 120138-B (See Model 650F)
Ch. 120140B (See Model 676B)
Ch. 120142B (See Model 686A)
Ch. 120143B, H (See Model 676F)
Ch. 120144B, G, H (See Model 676D)
Ch. 120149A (See Model 725A)
Ch. 120150-B (See Model 718B)
Ch. 120151 (See Model 734B)
Ch. 120152-B (See Model 731D)
Ch. 120152-F (See Model 733F)
Ch. 120153-B (See Model 700B)
Ch. 120154-B (See Model 794)
Ch. 120155A, B (See Model 705A, B)
Ch. 120158-B (See Model 740D)
Ch. 120160-B (See Model 699D)
Ch. 120162-A (See Model 709A)
Ch. 120163-D (See Model 716D)
Ch. 120164-B (See Model 718B)
Ch. 120165-D (See Model 735A)
Ch. 120167-D (See Model 731D)
Ch. 120168-D (See Model 716F)
Ch. 120169-B (See Model 711F)
Ch. 120169-D (See Model 720F)
Ch. 120169F (See Model 736F)
Ch. 120170-B (See Model 729B)
Ch. 120171-B (See Model 736B)
Ch. 120172A, B (See Model 737A, B)
Ch. 120173-D (See Model 740D)
Ch. 120174-B (See Model 752A)
Ch. 120175-B (See Model 748B)
Ch. 120176-B (See Model 745B)
Ch. 120177-B (See Model 746B)
Ch. 120178 (See Model 747)
Ch. 120180-D (See Model 753D)
Ch. 120182-D (See Model 741F)
Ch. 120184-B (See Model 755A)
Ch. 120185-B (See Model 712G)
Ch. 120190-D (See Model 760H)
Ch. 120191-D (See Model 760D)
Ch. 120192-B (See Model 787A)
Ch. 120192-D (See Model 771D)
Ch. 120192-F (See Model 775A)
Ch. 120193-B (See Model 758A)
Ch. 120193-F (See Model 726A)
Ch. 120194-D (See Model 757F)
Ch. 120195-D (See Model 785K)
Ch. 120198-B (See Model 731A)
Ch. 120197-F (See Model 784E)
Ch. 120197-D (See Model 784G)
Ch. 120198-D (See Model 753F)
Ch. 120199-B (See Model 778B)
Ch. 120201-B (See Model 738B)
Ch. 120206-D (See Model 781E)
Ch. 120208-D (See Model 1001E)
Ch. 120209-D (See Model 770C)
Ch. 120209-F (See Model 799E)

EMERSON-Cont.

Ch. 120210-D (See Model 766D)
Ch. 120211-D (See Model 771F)
Ch. 120211-F (See Model 793E)
EMPRESS
55, 56 7-14
ESPEY (Also see Philharmonic)
RR13, RR13L 13-17
78 47-8
78C 153-4
188 90-7
31 103-9
100 236-4
400, 500 241-7
200 242-4
200 247-6
400, 500 245-3
511C 174-6
512 68-8
512B 182-4
513, 514 63-8
524 90-7
581 14-10
621 10-17
641, 642 8-11
651 9-14
652, 653 (See Model 651-Set 9-14)
651 90-7
7511, 7, 5, 6514, 6516, 6517, 6520, 2, 6521, 6533 (Ch. FJ97) (See Model 651-Set 9-14)
6540, 6541 8-12
6542 (Ch. FJ97 (See Model 651-Set 9-14))
6545 (Ch. FJ97) 5-16
6546 (Ch. FJ97) (See Model 651-Set 9-14)
6547 (Ch. FJ97 (See Model 651-Set 9-14))
6560 (Ch. FJ97 (See Model 651-Set 9-14))
6611, 6612, 6613, 6614, 6615, 6620, 6631, 6632, 6634, 6635 (Ch. 97A) 18-16
7541 (Ch. FJ97) (See Model 651-Set 9-14)
7552 90-7
ESQUIRE
60-10, 65-4 14-11
511 157-3
517 (See Model 520-Set 163-5)
520 163-5
550 177-6
FADA
DL121 Tel. Rec. 200-5
DL121B Tel. Rec. (See Model 215C Ch. 12011-D) 200-5
G-925 Tel. Rec. 89-6
HD821 Tel. Rec. (See Model UH211-Set 228-10)
H212C Tel. Rec. (See Model UH211-Set 228-10)
H274T, H276T Tel. Rec. 247-5
H321T Tel. Rec. (See Model UH211-Set 228-10)
H421T Tel. Rec. (See Model UH211-Set 228-10)
H442C Tel. Rec. 247-5
H542C Tel. Rec. 247-5
H621T Tel. Rec. (See Model UH211-Set 228-10)
P80 27-9
P82 21-16
P100 27-10
P111 178-6
P130 135-7
R7C15, R7C25 Tel. Rec. 158-3
R-1025 Tel. Rec. 114-4
R-1050 Tel. Rec. 114-4
SAC20 Tel. Rec. 142-8
SAC40 Tel. Rec. 142-8
S4T15 Tel. Rec. 142-8
S4T30 Tel. Rec. 142-8
S6C55 Tel. Rec. 134-7
S6C70 Tel. Rec. 134-7
S6T65 Tel. Rec. 134-7
S7C20, S7C30 Tel. Rec. (See Model S6C55-Set 134-7)
S7C70 Tel. Rec. 134-7
S7T65 Tel. Rec. 134-7
S9C Tel. Rec. 134-7
S20120 Tel. Rec. (See Model S6C55-Set 134-7)
S1015 Tel. Rec. 109-4
S1020 Tel. Rec. 109-4
S1030 Tel. Rec. 109-4
S1051, S1055X Tel. Rec. 114-4
S1060 Tel. Rec. 134-7
S1065 Tel. Rec. 134-7
TV30 Tel. Rec. 74-3
UH21100T Tel. Rec. 228-10
UH211 Tel. Rec. 228-10
U1700CD Tel. Rec. 244-4
U1700D Tel. Rec. 244-4
U2100C, T Tel. Rec. 228-10
U2100C Tel. Rec. 228-10
V21T Tel. Rec. (See Model 215C-Set 200-5)
V2176 Tel. Rec. (See Model 215C-Set 200-5)
V217C Tel. Rec. (See Model DL121-Set 200-5)
V219C Tel. Rec. (See Model 215C-Set 200-5)
W424 Tel. Rec. 179-5
W52 Tel. Rec. 179-5
W732 Tel. Rec. 177-7
W776 Tel. Rec. 204-4
W779 Tel. Rec. 204-4
W20C22 Tel. Rec. 180-3
W2012 Tel. Rec. 180-3
W21C2 Tel. Rec. 200-5
W21T Tel. Rec. 200-5
W213 Tel. Rec. (See Model DL121-Set 200-5)
W214 Tel. Rec. (See Model 215C-Set 200-5)
W242 Tel. Rec. 200-5
W2410 Tel. Rec. 180-3
W73T, W75C, W77CD Tel. Rec. 192-5
W215C Tel. Rec. 200-5
W2012 Tel. Rec. 180-3
605, 606 Series 1-13
609, 610 Series 1-15

FADA-Cont.

633 17-13
637 17-14
652 Series 1-23
700 32-7
711 28-10
721 Tel. Rec. 177-7
740 28-10
7751 Tel. Rec. (See Model 7132-Set 177-7)
64-6
795 36-7
799 Tel. Rec. 74-3
830 97-5
845 97-6
855 92-2
880 Tel. Rec. 95A-5
899 Tel. Rec. 74-3
925 Tel. Rec. 89-6
930, 940 Tel. Rec. 74-3
965 Tel. Rec. 89-6
1000 Series 1-17
1001 17-15
FAIRMONT
30T14A-056 Tel. Rec. (Similar to Chassis) 119-3
38T17A-058 Tel. Rec. (Similar to Chassis) 109-1
317T3 Tel. Rec. (Similar to Chassis) 72-4
318T4 Tel. Rec. (Similar to Chassis) 85-3
318T45 Tel. Rec. (Similar to Chassis) 85-3
318T4-872 Tel. Rec. (Similar to Chassis) 85-3
318T6A Tel. Rec. (Similar to Chassis) 85-3
318T6A-950 Tel. Rec. (Similar to Chassis) 78-4
318T9A-800 Tel. Rec. (Similar to Chassis) 78-4
318T6A Tel. Rec. (Similar to Chassis) 85-3
318T9A-918 Tel. Rec. (Similar to Chassis) 78-4
318T10A-916 Tel. Rec. (Similar to Chassis) 78-4
2318T6A-954 Tel. Rec. (Similar to Chassis) 85-3
2318T9A-912 Tel. Rec. (Similar to Chassis) 78-4
FARNSWORTH (Also see Record Changer Listing)
EC-260 7-15
EK-081, EK-082, EK-083, 26-13
EK-262, EK-263BL, E-263WL, E-264BL, EK-264WL, EK-265 7-15
EK-681 26-13
ET-060, ET-061, ET-063, 6-11
ET-064, ET-065, ET-066 4-2
GK-100, GK-102, GK-103, GK-104 23-8
GK-111, GK-112, GK-114, GK-115 60-11
GK-140, GK-141, GK-142, GK-143, GK-144 24-18
GT-050, GT-051, GT-052, 35-5
GT-060, GT-061, GT-064, GT-065 35-6
K-267, K-669 (See Model EC-260-Set 7-15)
Ch. 150 (See Model ET-060)
Ch. 152, 153 (See Model EC-260)
Ch. 156, 157 (See Model EK-081)
Ch. 158, 159 (See Model ET-064)
Ch. 162 (See Model EC-260)
Ch. 170 (See Model GK-100)
Ch. 193 (See Model EK-081)
Ch. 194, 201, 216 (See Model GK-100)
FEDERAL MFG. CO.
104 (Select-A-Call) 18-17
135 (Select-A-Call) 11-7
FEDERAL TEL. & RADIO CORP.
1021 (See Model 1030T-Set 8-13)
1030T 8-13
1031, 1032 (See Model 1030T-Set 8-13)
1040T 23-9
1040TB (See Model 1040T-Set 23-9)
1540T 8-13
FEDWAY
321MS39A Tel. Rec. (Similar to Chassis) 226-11
2321MS39A Tel. Rec. (Similar to Chassis) 226-11
FERRAR
C-81-B 17-16
T-618 39-4
WR-11 15-10
FIRESTONE (AIR CHIEF)
A-2 (Code No. 297-6-LMMU-143) 14-4
A-3 (Code No. 297-6-LMMU-134) 31-23
A-4 (Code No. 297-7-RV228) 28-11
A-4-11 (Code No. 188-8-4A11) 41-7
A-4-12 (Code No. 213-8-8370) 49-9
A-4-15 (Code 177-7-4A15) 36-7
A-4-17 (Code No. 213-7-7270) 35-7
A-4-20 (Code 5-5-9000-A) 15-11
A-4-21 (Code No. 5-5-9001-A) 11-19
A-4-22X (Code No. 5-5-9001-B) 11-19
A-4-23 (5-5-9003-A) 2-29
A-4-24 (Code 291-6-566) 13-5
A-4-25 (Code 291-6-572) 13-6
A-4-26 (Code 307-6-9030-A) 33-5
A-4-27 28-12
A-4-31 (Code No. 177-5-4A31) 11-20
A-4-37 (Code 177-5-4A37) 13-7
A-4-41 (Code 291-7-576) 52-8
A-4-42 (Code No. 177-7-4A42) 30-9

FIRESTONE-Cont.

4-A-60 (Code No. 307-8-9047A) 38-5
4-A-61 (Code No. 332-8-13712T) 48-7
4-A-62, 4-A-63 67-10
4-A-64, 4-A-65 68-9
4-A-66 (Code No. 177-8-4A66) 74-4
4-A-68 (Code No. 332-8-143653) 53-11
4-A-69 (Code No. 155-8-85) 61-8
4-A-70 136-8
4-A-71 (Code 291-8-628) 59-9
4-A-78, 4-A-79 117-5
4-A-80 118-7
4-A-86 129-6
4-A-86 (Lots) 144-4
4-A-87 119-7
4-A-88 132-6
4-A-89 118-7
4-A-92 154-4
4-A-95 144-4
4-A-96 (See Model 4-A-87-Set 119-7)
4-A-97, 4-A-98 147-5
4-A-101, 4-A-102 181-7
4-A-108 (Code 297-2-361) 191-8
4-A-110 215-6
4-A-112 (See Model 4-A-92-Set 154-4)
4A-113, 4A-114 224-8
4-A-115 219-5
4-A-118 (See Model 4-A-92-Set 119-7)
4-A-121, 4-A-122 244-5
4-B-1 (Code 7-6-PM15) 7-1
4-B-2 (Code 7-6-PM14) 18-18
4-B-6 (Code No. 177-7-PM18) 29-8
4-B-56 133-4
4-B-57 124-4
4-B-58 135-8
4-B-60 153-5
4-B-61 155-6
4-B-62 152-6
4-B-63 (Similar to Chassis) 17-4
4-B-67 (Code 120-2-F152) 167-6
4-B-69 235-6
4-B-71 222-6
4-B-72 223-7
4-C-3 19-17
4-C-5 (Code 291-7-574) 19-17
4-C-6 19-17
4-C-13 (Code 332-8-140623) 66-9
4-C-16, 4-C-17 120-6
4-C-18 110-8
4-C-19, 4-C-20 170-7

FORD-HALLICRAFTERS

FORD-Cont.

FAD-18805-D	208-6
FAE-18805-A	215-7
FDA-18805-B1	236-5
FDA-18805-B-2	250-10
GF890, E (OA-18805-B)	109-5
M-1 (FA-18805-A1)	46-4
M-1A (OA-18805-A1) [See Model M-1-Set 46-4]	
M-1A-1 (OA-18805-A1)	106-8
M-2 (1A-18805-A1)	132-7
M-4 (FAC-18805-A1)	184-7
M-4A (FAC-18805-C) [See Model M-4-Set 184-7]	
M-4B (FAD-18805-B1)	236-5
OA-18805-A1 [See Model M-1A or Model M-1A-1]	
OA-18805-A2	135-9
OA-18805-B	109-5
OBF (OA-18805-A1) [Serial No. 150,000 and below] [See Model M-1-Set 46-4]	
OBF (OA-18805-A1) [Serial No. 150,001 and up] [See Model M-1A-1-Set 106-8]	
OCF751-1 (1A-18805-D)	157-4
OMF (OA-18805-A2)	135-9
OZF (OA-18805-A1) [See Model GF890-Set 109-5]	
1A-18805-A1	132-7
1A-18805-A2	131-8
1A-18805-B [See Model 1CF743-Set 133-7 or Model 1CF743-1-Set 158-5]	
1A-18805-D	157-4
1A-18805-G	157-4
1BF (1A-18805-A1) [See Model M-2-Set 132-7]	
1CF743 (1A-18805-B)	133-7
1CF743-1 (1A-18805-B)	158-5
1CF751-2 (1A-18805-G)	157-4
1MF (1A-18805-A2)	131-8
1SFT751-2 (1A-18805-G) [See Model 1CF751-2-Set 157-4]	
2BF (FAC-18805-A1) [See Model M-4-Set 184-7]	
2CF754 (FAC-18805-B)	167-7
2MF (FAC-18805-A)	175-10
3BF (FAD-18805-C) [See Model M-4-Set 184-7]	
3MF (FAD-18805-C)	206-5
3MFF (FAE-18805-A)	215-7
3S755 (FAD-18805-D)	208-6
4BF (See Model M-4B-Set 236-5)	
4MF (FAD-18805-B-2)	250-10
6MF800 (51A-18805-A1) (Ch. 60A1)	10-18
6MF780 (51A-18805-A1)	62-12
6MF780-E (51AF-18805) [See Model 6MF780-Set 62-12]	
8A-18805	83-4
8A-18805-A	44-4
8A-18805-A1	46-4
8A-18805-A3 [See Model 9A-Set 46-4]	
8A-18805-B [See Model 8BF880-Set 42-12 or Model 8BF980-Set 61-9]	
8A-18805-B1	83-4
8C-18805-B	47-9
8BF880 (8A-18805-B)	42-12
8BF881 (8C-18805-B)	47-9
8BF980 (8A-18805-B)	61-9
8BF983 (8A-18805-1), 8BF983-E (8A-18805)	83-4
8ZT (8C-18805-B) [See Model 8BF881-Set 42-12]	
9BF (8A-18805-A1) [See Model M-1-Set 46-4]	
9DF (8A-18805-A) [See Model 8072-Set 44-4]	
9MF (8A-18805-A3) [See Model 8072-Set 44-4]	
9ZF (8A-18805-B1) [See Model 8BF983-Set 83-4]	
51AF-18805 [See Model 6MF780-E]	
51A-18805-A1 [See Model 6MF800-Set 10-18 or Model 6MF780-Set 62-12]	
51A-18805-B2	45-10
7070 (51A-18805-B2)	45-10
8072 (8A-18805-A)	44-4

FREED EISEMAN

46	11-8
54, 55, 56, 68 (Ch. 1620C) Tel. Rec.	113-1A

GALVIN (See Motorola)

GAMBLE-SKOGMO (See Coronado)

GAROD (Also see Majestic)

4A1, 4A-2	29-9
4B1	51-6
5A-1	22-15
5A-2	5-28
5A-3	44-5
5A-4	40-6
5AP1-Y "The Companion"	15-12
5D, 5D-2	12-12
5D-3, 5D-3A	22-16
5D-4, 5D-5	33-7
5RC-1	36-8
6A-2	28-13
6A-1	5-29
6BU-1A "The Senator"	13-18
6DPS, 6DPS-A	12-13
10T21, 10T22, 10T23, 10T25 Tel. Rec.	60-12
10T220, 10T221, 10T222, 10T223 Tel. Rec.	95A-4
11FMP	38-7
12T21, 12T22, 12T23, 12T24, 12T25, 12T26A, 12T27A Tel. Rec.	60-12
12T220, 12T221, 12T222, 12T223 Tel. Rec.	95A-4
15T26, 15T27 Tel. Rec.	60-12
15T224, 15T225, 15T226, 15T227 Tel. Rec.	95A-4
16CT4, 16CT5 Tel. Rec. [See Majestic Model 16CT4-Set 133-8]	
19C6, 19C7 Tel. Rec. [See Majestic Model 19C6-Set 133-8]	
62B	29-10
30A	48-8
900TV, 910TV Tel. Rec.	50-7
1002TV, 1010TV Tel. Rec.	50-7
1042G, 1043G Tel. Rec. [See Majestic Model 12C4-Set 108-7]	

GAROD-Cont.

1042T, 1043T Tel. Rec.	93A-7
1100TVP, 1110TVP Tel. Rec.	50-7
1200TVP, 1210TVP Tel. Rec.	50-7
1244G, 1245G Tel. Rec. [See Majestic Model 12C4-Set 108-7]	
1244T, 1245T Tel. Rec.	93A-7
1246G, 1247G Tel. Rec. [See Majestic Model 12C4-Set 108-7]	
1546T, 1547T Tel. Rec.	93A-7
1548G, 1549G Tel. Rec. [See Majestic Model 12C4-Set 108-7]	
1671 (98 Series) Tel. Rec.	971-3
1671, 1672, 1673, 1674 Tel. Rec. [See Majestic Model 1671-Set 133-8]	
1974, 1975 Tel. Rec. [See Majestic Model 1974-Set 133-8]	
2042T, 2043T Tel. Rec.	93A-7
2546T Tel. Rec.	93A-7
2549T Tel. Rec.	93A-7
3912 TVFMP, 3915 TVFMP Tel. Rec.	95A-6

GARRARD (See Record Changer Listing)

GENERAL (Mutual Buying Syndicate)

17CG1, 17TV Tel. Rec. [Similar to Chassis]	149-13
--	--------

GENERAL ELECTRIC (Also see Record Changer Listing)

A1-200	243-6
A1-300	238-8
UHF-03 Tel. UHF Conv.	209-5
YR8-60-1, YR8-60-2, YR8-60-12	33-8
10C101, 10C102 Tel. Rec.	96-4
10T1 Tel. Rec.	96-4
10T4, 10T5, 10T6 Tel. Rec.	96-4
12C101, 12C102, 12C105 Tel. Rec.	96-4
12C107, 12C107B, 12C108, 12C-108B, 12C109, 12C109B Tel. Rec.	125-7
12K1 Tel. Rec.	95A-6
12T1 Tel. Rec.	96-4
12T3, 12T3B, 12T4, 12T4B Tel. Rec.	125-7
12T7 Tel. Rec.	99A-5
14	35-8
14C102, 14C103 Tel. Rec.	123-4
14T2, 14T3 Tel. Rec.	123-4
16C103 Tel. Rec.	123-4
16C110, 16C111 Tel. Rec.	123-4
16C113 Tel. Rec.	123-4
16C115, 16C116, 16C117 Tel. Rec.	123-4
16K1, 16K2 Tel. Rec.	161-1A
16T1, 16T2, 16T3, 16T4 Tel. Rec.	161-1
16T5 Tel. Rec. [See Model 16T4-Set 123-4]	
17C101, 17C102 Tel. Rec.	123-4
17C103, 17C104, 17C105 Tel. Rec. [Also see PCB 32-Set 158-11]	
17C106	141-6
17C107, 17C108, 17C109 Tel. Rec. [Also see PCB 32-Set 158-11]	
17C110, 17C111 [Early, "D" and "E" Versions] Tel. Rec.	180-5
17C112 Tel. Rec. [See PCB 32-Set 158-11 and Model 17C103-Set 141-6]	
17C113 Tel. Rec.	166-10
17C114 Tel. Rec. [See PCB 32-Set 158-11 and Model 17C103-Set 141-6]	
17C115 Tel. Rec.	166-10
17C117 Tel. Rec. [See Model 17C-113-Set 166-10]	
17C120 Tel. Rec.	166-10
17C125 Tel. Rec. [See PCB 64-Set 201-1 and Model 21C201-Set 194-2]	
17C125-UHF Tel. Rec. [For TV Ch. see PCB 64-Set 201-1 and Model 21C201-Set 194-2, for UHF Conv. see Model UHF-103-Set 209-5]	
17C127 Tel. Rec. [See PCB 97-Set 242-1 and Model 21C115-Set 229-7]	
17T1, 17T2, 17T3 Tel. Rec. [Also see PCB 32-Set 158-11, 141-6]	
17T4, 17T5, 17T6 Tel. Rec. [See PCB 32-Set 158-11 and Model 17C103-Set 141-6]	
17T7 Tel. Rec. [See Model 17C113-Set 166-10]	
17T10 Tel. Rec.	196-3
17T10-UHF Tel. Rec. [For TV Ch. see Model 17T10-Set 196-3, for UHF Conv. see Model UHF-103-Set 209-5]	
17T11 Tel. Rec. [See Model 17T10-Set 196-3]	
17T11-UHF Tel. Rec. [For TV Ch. see Model 17T11-Set 196-3, for UHF Conv. see Model UHF-103-Set 209-5]	
17T12 Tel. Rec. [See Model 17T10-Set 196-3]	
17T12-UHF Tel. Rec. [For TV Ch. see Model 17T12-Set 196-3, for UHF Conv. see Model UHF-103-Set 209-5]	
17T15, 17T17 Tel. Rec. [See PCB 97-Set 242-1 and Model 21C115-Set 229-7]	
19C101 Tel. Rec.	99A-6
20C105, 20C106 Tel. Rec.	176-3
20C107-UHF Tel. Rec. [See PCB 64-Set 201-1 and Model 21C201-Set 194-2]	
20C107-UHF Tel. Rec. [For TV Ch. see PCB 64-Set 201-1 and Model 21C201-Set 194-2, for UHF Conv. see Model UHF-103-Set 209-5]	
20C150, 20C151 Tel. Rec.	153-6
20T2 Tel. Rec.	176-3
21C114 Tel. Rec. [See PCB 97-Set 242-1 and Model 21C115-Set 229-7]	
21C115 Tel. Rec. [Also see PCB 97-Set 242-1]	229-7

GENERAL ELECTRIC-Cont.

21C116, 21C117 Tel. Rec. [See PCB 97-Set 242-1 and Model 21C115-Set 229-7]	
21C120, 21C121 Tel. Rec. [See PCB 97-Set 242-1 and Model 21C115-Set 229-7]	
21C201 Tel. Rec.	176-3
21C201-UHF Tel. Rec. [Also see PCB 64-Set 201-1]	194-2
21C201-UHF Tel. Rec. [For TV Ch. see PCB 64-Set 201-1 and Model 21C201-Set 194-2, for UHF Conv. see Model UHF-103-Set 209-5]	
21C202 Tel. Rec. [Also see PCB 64-Set 201-1]	194-2
21C202-UHF Tel. Rec. [For TV Ch. see PCB 64-Set 201-1 and Model 21C201-Set 194-2, for UHF Conv. see Model UHF-103-Set 209-5]	
21C204 Tel. Rec. [Also see PCB 64-Set 201-1]	194-2
21C205 Tel. Rec. [Also see PCB 64-Set 201-1]	194-2
21C206-UHF Tel. Rec. [For TV Ch. see PCB 64-Set 201-1 and Model 21C206-Set 194-2, for UHF Conv. see Model UHF-103-Set 209-5]	
21C208 Tel. Rec. [Also see PCB 64-Set 201-1]	194-2
21C208-UHF Tel. Rec. [For TV Ch. see PCB 64-Set 201-1 and Model 21C208-Set 194-2, for UHF Conv. see Model UHF-103-Set 209-5]	
21C208UHF Tel. Rec. [See PCB 64-Set 201-1 and Model 21C208-Set 194-2]	
21C208UHF Tel. Rec. [For TV Ch. see PCB 64-Set 201-1 and Model 21C208-Set 194-2, for UHF Conv. see Model UHF-103-Set 209-5]	
21C210-UHF Tel. Rec. [For TV Ch. see PCB 64-Set 201-1 and Model 21C210-Set 194-2, for UHF Conv. see Model UHF-103-Set 209-5]	
21C212 Tel. Rec. [Also see PCB 64-Set 201-1]	194-2
21C212-UHF Tel. Rec. [For TV Ch. see PCB 64-Set 201-1 and Model 21C212-Set 194-2, for UHF Conv. see Model UHF-103-Set 209-5]	
21C214-UHF Tel. Rec. [Also see PCB 64-Set 201-1]	194-2
21C214-UHF Tel. Rec. [For TV Ch. see PCB 64-Set 201-1 and Model 21C214-Set 194-2, for UHF Conv. see Model UHF-103-Set 209-5]	
21C225, 21C226, 21C227, 21C228, 21C229, 21C230, 21C231, 21C232, 21C233, Tel. Rec.	194-2
21T1 Tel. Rec. [Also see PCB 64-Set 201-1]	194-2
21T1-UHF Tel. Rec. [For TV Ch. see PCB 64-Set 201-1 and Model 21T1-Set 194-2, for UHF Conv. see Model UHF-103-Set 209-5]	
21T1U Tel. Rec. [See PCB 64-Set 201-1 and Model 21T1-Set 194-2]	
21T1U-UHF Tel. Rec. [For TV Ch. see PCB 64-Set 201-1 and Model 21T1U-Set 194-2, for UHF Conv. see Model UHF-103-Set 209-5]	
21T2 Tel. Rec.	196-3
21T3 Tel. Rec. [See Model 21T1-Set 194-2]	
21T3-UHF Tel. Rec. [For TV Ch. see PCB 64-Set 201-1 and Model 21T3-Set 194-2, for UHF Conv. see Model UHF-103-Set 209-5]	
21T4, 21T5 Tel. Rec.	184-8
21T6 Tel. Rec. [See Model 21T1-Set 194-2]	
21T6-UHF Tel. Rec. [For TV Ch. see PCB 64-Set 201-1 and Model 21T6-Set 194-2, for UHF Conv. see Model UHF-103-Set 209-5]	
21T7, 21T8 Tel. Rec.	225-10
21T11, 21T12 Tel. Rec. [See PCB 97-Set 242-1 and Model 21C115-Set 229-7]	
21T14 Tel. Rec. [Also see PCB 97-Set 242-1]	229-7
21T20, 21T21 Tel. Rec.	237-7
24C101 Tel. Rec.	152-8
41, 42, 43, 44, 45	32-8
50	7-16
60, 62	36-9
64, 65	98-4
66, 67	76-12
100, 101	61-3
102, 102W	41-3
103, 105	61-3
106	8-14
107, 107W	41-8
113	51-7
114, 114W, 115, 115W	41-8
118, 119W, 119W	61-3
123, 124	97-7
131 [See Model 118-Set 39-5]	
135, 136	81-8
140	30-10
143	75-9
145	65-13
150	56-11
150	56-12
165	89-7
180	20-11
186-4	57-9
200, 201, 202, 203, 205, 205M	8-15
210, 211, 212	51-8
218, 218 "H"	121-5
219, 220, 221	4-1
226	91-5
230 [See Kaiser-Frazer Model 200001-Set 35-13]	
250	4-13
254	32-9
258	15-13
280	23-10
303	18-19

GENERAL ELECTRIC-Cont.

304	32-10
321	3-26
324	6-7
326, 327	30-11
328	64-7
329, 330 [See Model 324-Set 64-7]	
354, 355	33-9
356, 357, 358	37-6
376, 377, 378	45-11
400, 401	118-8
404, 405	121-6
408	116-6
409	121-6
410	121-6
411	118-8
412	189-9
412F	211-6
414	175-11
414F	211-6
415	175-11
415F	211-6
416	175-11
416F	211-6
417	16-15
419	231-8
422, 423	154-5
424, 425	233-2
430	175-11
432, 432	241-9
440	246-6
450, 451, 452 [See Model 424-Set 233-2]	
500, 501	98-4
502	35-9
505, 506, 507, 508, 509	98-4
510, 511	123-5
510F, 511F, 512F, 513F	143-7
514	198-7
515F, 516F, 517F, 518F	143-7
521, 522	114-5
521F, 522F	143-7
530	93-4
535	151-7
542, 543	198-7
546, 547, 548, 549	191-9
551, 552	201-4
555, 555G, 556	250-11
557, 558, 559 [See Model 560-Set 249-7]	
560, 561	249-7
564, 565, 566	251-7
600	109-6
601, 603, 604	115-3
605, 606	145-6
607, 608 [See Model 605-Set 145-6]	
610, 611	147-7
612, 613	231-9
614, 615	199-6
625, 626 [See Model 612-Set 231-9]	
640, 641 [See Model 614-Set 199-6]	
650	101-3
741	157-6
752, 753	63-9
754	167-8
755	130-6
756	167-8
757 [See Model 755-Set 130-6]	
800A, B, C, D Tel. Rec. [See Model 800-Set 78-7]	
802 Tel. Rec.	91A-7
803 Tel. Rec.	97A-4
805, 806, 807, 809 Series Tel. Rec.	78-7
810 Tel. Rec.	53-12
811 Tel. Rec.	63-9
814 Tel. Rec.	69-9
815 Tel. Rec.	97A-5
817 Tel. Rec.	78-7
818 Tel. Rec.	95A-7
821 Tel. Rec.	78-7
830 Early, Tel. Rec.	81-9
835 Early, Tel. Rec.	81-9
840 Tel. Rec.	81-9
901 Tel. Rec.	97A-5
910 Tel. Rec.	97A-5

GENERAL IMPLEMENT

9A5	37-7
-----	------

GENERAL INDUSTRIES (See Changer and Recorder Listings)

GENERAL INSTRUMENT (Also see Recorder Changer Listing)

63A, 64 Tel. UHF Conv.	232-7
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GENERAL MOTORS CORP. (GMC)

2233029	93-6
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GENERAL TELEVISION

1A5, 2A5, 3A5, 5A5 (Ch. 1-1)	1-21
4B5	27-11
5B5G, 5B5Y	

HALLICRAFTERS—Cont.

511 Tel. Rec.	96-5
512, 513 Tel. Rec.	80-7
514 Tel. Rec.	91-6
515 Tel. Rec.	80-7
518, 519, 520 Tel. Rec.	92-3
520E Tel. Rec.	80-7
521 Tel. Rec.	92-3
521E Tel. Rec.	80-7
524 Tel. Rec.	80-7
600, 601, 602, 603, 604 Tel. Rec.	92-3
605, 606 Tel. Rec.	107-5
611, 612	250-12
680, 611 Tel. Rec.	113-3
690 Tel. Rec.	113-3
715, A Tel. Rec.	113-3
716 Tel. Rec. (See Model 680—Set 113-3)	
730, 731 (Run 1) Tel. Rec. (See Model 680—Set 113-3)	
741, 741 (Run 1) Tel. Rec. (See Model 680—Set 113-3)	
745 Tel. Rec.	105-4
750, 751 Tel. Rec.	105-4
760, 751 Tel. Rec.	105-4
805, 806 Tel. Rec.	136-9
810 Tel. Rec.	136-9
810A, 811 Tel. Rec.	124-6
815 Tel. Rec.	124-6
818, 820 Tel. Rec.	124-6
821 Tel. Rec. (See Model 810A—Set 124-6)	
822 Tel. Rec.	124-6
832, 833 Tel. Rec.	124-6
860, 861 Tel. Rec.	124-6
870, 871 Tel. Rec. (See Model 810A—Set 124-6)	
880 Tel. Rec. (See Model 810A—Set 124-6)	
1000 (Ch. W1000D) Tel. Rec.	180-7
1001 (Ch. F1100D) (See Model 1000—Set 169-7)	
1002, 1003, 1004 (Ch. F1100D) Tel. Rec.	169-7
1005, 1006 (Ch. A1100D) Tel. Rec.	177-3
1007 (Ch. F1100D) Tel. Rec.	169-7
1008 (Ch. X1000D) Tel. Rec.	180-7
1010P (Ch. A-1200D, K1200D, W1300D) Tel. Rec.	188-6
1012P (Ch. A-1200D, K1200D, W1300D) Tel. Rec.	188-6
1013C (Ch. F1200D) Tel. Rec.	188-6
1015, 1016, 1017, 1018, 1019 (Ch. A1100D) Tel. Rec.	177-3
1019 (Ch. Z1000D) Tel. Rec.	180-7
1021P (Ch. D1200D, L1200D, X1200D) Tel. Rec.	188-6
1022C (Ch. G1200D) Tel. Rec.	188-6
1025 (Ch. C1000D) Tel. Rec.	172-4
1026P (Ch. D1200D, L1200D, X1200D) Tel. Rec.	188-6
1027C (Ch. G1200D) Tel. Rec.	188-6
1050, A (Ch. A11200D) Tel. Rec. (Also see PCB 81—Set 222-1)	
1051P, 1052P (Ch. P1200D) Tel. Rec. (See PCB 75—Set 216-1 and Model 1010P—Set 188-6)	
10531, 1054P (Ch. R1200D) Tel. Rec. (See PCB 75—Set 216-1 and Model 1010P—Set 188-6)	
1055C, 1056C (Ch. T1200D) Tel. Rec. (See PCB 75—Set 216-1 and Model 1010P—Set 188-6)	
1060C, 1061C (Ch. T1200D) Tel. Rec. (See PCB 75—Set 216-1 and Model 1010P—Set 188-6)	
1062C, 1063C (Ch. J1200D) Tel. Rec. (See PCB 75—Set 216-1 and Model 1010P—Set 188-6)	
1072 (Ch. AG1200D) Tel. Rec.	211-7
1072A (Ch. AR1200D) Tel. Rec.	211-7
1074 (Ch. AG1200D) Tel. Rec.	211-7
1074A (Ch. AR1200D) Tel. Rec.	211-7
1074AT (Ch. AY1200D) Tel. Rec. (Also see PCB 81—Set 222-1)	
1075 (Ch. AG1200D) Tel. Rec.	211-7
1075A (Ch. AR1200D) Tel. Rec.	211-7
1075AT (Ch. AY1200D) Tel. Rec. (Also see PCB 81—Set 222-1)	
1077 (Ch. AH1200D) Tel. Rec.	211-7
1078 (Ch. AG1200D) Tel. Rec.	211-7
1078A (Ch. AR1200D) Tel. Rec.	211-7
1078AT (Ch. AY1200D) Tel. Rec. (Also see PCB 81—Set 222-1)	
1081, A (Ch. AJ1200D) Tel. Rec. (Also see PCB 81—Set 222-1)	
1081B (Ch. AZ1200D) Tel. Rec. (See PCB 81—Set 222-1 and Model 1050—Set 211-7)	
1081C (Ch. BA1200D) Tel. Rec. (See PCB 81—Set 222-1 and Model 1050—Set 211-7)	
1081D (Ch. AZ1200D) Tel. Rec. (See PCB 81—Set 222-1 and Model 1050—Set 211-7)	
1081E (Ch. BA1200D) Tel. Rec. (See PCB 81—Set 222-1 and Model 1050—Set 211-7)	
1085A (Ch. AJ1200D) Tel. Rec. (Also see PCB 81—Set 222-1)	
1085B (Ch. AZ1200D) Tel. Rec. (See PCB 81—Set 222-1 and Model 1050—Set 211-7)	
1085C (Ch. BA1200D) Tel. Rec. (See PCB 81—Set 222-1 and Model 1050—Set 211-7)	

HALLICRAFTERS—Cont.

1085D (Ch. AZ1200D) Tel. Rec. (See PCB 81—Set 222-1 and Model 1050—Set 211-7)	
1085E (Ch. BA1200D) Tel. Rec. (See PCB 81—Set 222-1 and Model 1050—Set 211-7)	
1088A (Ch. AJ1200D) Tel. Rec. (Also see PCB 81—Set 222-1)	
1088B (Ch. AZ1200D) Tel. Rec. (See PCB 81—Set 222-1 and Model 1050—Set 211-7)	
1088C (Ch. BA1200D) Tel. Rec. (See PCB 81—Set 222-1 and Model 1050—Set 211-7)	
1088D (Ch. AZ1200D) Tel. Rec. (See PCB 81—Set 222-1 and Model 1050—Set 211-7)	
1092 (Ch. AZ1200D) Tel. Rec. (See PCB 81—Set 222-1 and Model 1050—Set 211-7)	
1111P (Ch. A1200D) Tel. Rec.	188-6
1113P (Ch. D1200D) Tel. Rec.	188-6
14808 (Ch. R9000) Tel. Rec.	167-10
17804C Tel. Rec.	155-8
17810M Tel. Rec.	152-9
17811-H Tel. Rec.	156-6
17812, 17813, 17814, 17815-H Tel. Rec.	155-8
17816, 17817 Tel. Rec.	156-6
17819 Tel. Rec.	155-8
17824 Tel. Rec.	155-8
17824-A Tel. Rec.	155-6
17825 Tel. Rec. (See Model 17804C—Set 155-8)	
17829 (Ch. F1100D) Tel. Rec. (See Model 1000—Set 169-7)	
17838 Tel. Rec.	155-8
17848, 17849, 17850 Tel. Rec.	155-8
17860-H, 17861-H Tel. Rec.	156-6
17905 Tel. Rec. (See Model 17810—Set 152-9)	
17906 Tel. Rec.	165-6
17908 Tel. Rec. (See Model 17824-A—Set 165-6)	
17922 Tel. Rec. (See Model 17824-A—Set 165-6)	
17930, 17931, 17932, 17933, 17934 Tel. Rec.	165-6
20823 (Ch. M9000D) Tel. Rec.	167-10
20823B (Ch. L9000D) Tel. Rec.	167-10
20823C Tel. Rec.	165-6
20882 Tel. Rec.	155-8
20990, 20990S, 20994 Tel. Rec.	154-6
21923 Tel. Rec.	165-6
21928 Tel. Rec.	165-6
21940 Tel. Rec.	165-6
21980 Tel. Rec.	165-6
Ch. A1100D (See Model 1005)	
Ch. A1200D (See Model 1010P)	
Ch. AG1200D (See Model 1072)	
Ch. AH1200D (See Model 1077)	
Ch. AJ1200D (See Model 1081)	
Ch. AL1200D (See Model 1050)	
Ch. AR1200D (See Model 1072A)	
Ch. AX1200D (See Model 1092)	
Ch. AY1200D (See Model 1074AT)	
Ch. AZ1200D (See Model 1081B)	
Ch. BA1200D (See Model 1081C)	
Ch. D1200D (See Model 1021P)	
Ch. F1200D (See Model 1013C)	
Ch. G1200D (See Model 1022C)	
Ch. J1200D (See Model 1062C)	
Ch. K1200D (See Model 1010P)	
Ch. L1200D (See Model 1021P)	
Ch. P1200D (See Model 1051P)	
Ch. R1200D (See Model 14808)	
Ch. T1200D (See Model 1055C)	
Ch. W1000D (See Model 1000)	
Ch. W1200D (See Model 1010P)	
Ch. X1000D (See Model 1008)	
Ch. X1200D (See Model 1031P)	
Ch. Z1000D (See Model 1019)	

HAMILTON ELECTRONICS

H-15-S	16-17
H-50-2S	16-18

HAMILTON RADIO CORP. (See Olympic)

HAMMARLUND

HQ-129-X	8-18
SP-400-X	10-20

HARVEY-WELLS

AT-3B-6, AT-3B-12	32-11
ATR-3-6, ATR-3-12	36-14

HEATH

HBR-5	24-20
-------	-------

HOFFMAN

A-200 (Ch. 103)	4-23
A-202 (Ch. 119)	11-11
A-300	4-41
A-309 (Ch. 119)	11-11
A-401 (Ch. 102)	11-12
A-500 (Ch. 107)	4-34
A-501 (Ch. 085)	5-19
A-700 (Ch. 110S)	12-16
B-400	17-17
B-1000	20-14
C-501	105-11
C-502	51-9
C-503	40-9
C-504 (Ch. 123)	47-10
C-506, C-507	49-10
C-511	48-11
C-512	51-9
C-513	50-9
C-514	47-10
C-518	61-13
C710 (Ch. 133)	
C1006, C1007	54-9
CT-800, CT-801, CT-900, CT-901	63-11
78104 (Ch. 190, B) Tel. Rec.	201-5
78108 (Ch. 210, M) Tel. Rec.	205-5
78113 (Ch. 202) Tel. Rec.	205-5

HOFFMAN—Cont.

78138 (Ch. 212, M) Tel. Rec.	194-4
78128 (Ch. 212) Tel. Rec. (See Model 78138—Set 194-4)	
78141, U (Ch. 300-21) Tel. Rec.	236-6
78303 (Ch. 190, B) Tel. Rec.	201-5
7M103 (Ch. 190, B) Tel. Rec.	201-5
7M109 (Ch. 202) Tel. Rec.	205-5
7M109B (Ch. 210, M) Tel. Rec.	205-5
7M112 (Ch. 202) Tel. Rec.	205-5
7M112B (Ch. 212, M) Tel. Rec.	194-4
7M127 (Ch. 212) Tel. Rec. (See Model 78138—Set 194-4)	
7M140, U (Ch. 300-21) Tel. Rec.	236-6
7M302 (Ch. 190, B) Tel. Rec.	201-5
7P105 (Ch. 190, B) Tel. Rec.	201-5
7P118 (Ch. 210, M) Tel. Rec.	205-5
7P148 (Ch. 212, M) Tel. Rec. (See Model 78138—Set 194-4)	
7P304 (Ch. 190, B) Tel. Rec.	201-5
20B102 (Ch. 183T) Tel. Rec.	168-8
20B102F (Ch. 194) Tel. Rec.	201-5
20B501 (Ch. 183T) Tel. Rec.	168-8
20M101 (Ch. 183T) Tel. Rec.	168-8
20M101F (Ch. 194) Tel. Rec.	201-5
20M500 (Ch. 183T) Tel. Rec.	168-8
20P502 (Ch. 183T) Tel. Rec.	168-8
21B107 (Ch. 191, B) Tel. Rec.	201-5
21B116 (Ch. 196, M) Tel. Rec.	195-8
21B122 (Ch. 211, M) Tel. Rec.	194-4
21B134 (Ch. 211, M) Tel. Rec. (See Model 21B122—Set 194-4)	
21B137 (Ch. 196) Tel. Rec. (See Model 21B116—Set 195-8)	
21B144, U (Ch. 300-21) Tel. Rec.	236-6
21B147, U (Ch. 401-21) Tel. Rec.	249-8
21B161, U (Ch. 406-21) Tel. Rec.	250-13
21B301 (Ch. 191, B) Tel. Rec.	201-5
21B306B (Ch. 211, M) Tel. Rec.	194-4
21B309 (Ch. 196M, T) Tel. Rec.	195-8
21B315 (Ch. 211T) Tel. Rec. (See Model 21B122—Set 194-4)	
21B318, U (Ch. 300-21) Tel. Rec.	236-6
21B321, U (Ch. 401-21) Tel. Rec.	249-8
21B331, U (Ch. 405-21) Tel. Rec.	250-13
21B334, U (Ch. 405-21) Tel. Rec.	250-13
21B504 (Ch. 191, B) Tel. Rec.	201-5
21B507 (Ch. 211, M) Tel. Rec.	194-4
21B510, T (Ch. 196) Tel. Rec. (See Model 21B116—Set 195-8)	
21B701 (Ch. 191, B) Tel. Rec.	201-5
21B701 (Ch. 196M, T) Tel. Rec.	195-8
21B716 (Ch. 211T) Tel. Rec. (See Model 21B122—Set 194-4)	
21B719, U (Ch. 300-21) Tel. Rec.	236-6
21B723, U (Ch. 401-21) Tel. Rec.	249-8
21B901 (Ch. 192) Tel. Rec. (Ch. only)	201-5
21B904 (Ch. 213, M) Tel. Rec.	211-8
21B907 (Ch. 199, M, T and Radio Ch. 182) Tel. Rec.	221-6
21M106 (Ch. 191, B) Tel. Rec.	201-5
21M115 (Ch. 196, M) Tel. Rec.	195-8
21M121 (Ch. 211, M) Tel. Rec.	194-4
21M133 (Ch. 211) Tel. Rec. (See Model 21B122—Set 194-4)	
21M136 (Ch. 196) Tel. Rec. (See Model 21B116—Set 195-8)	
21M143, U (Ch. 300-21) Tel. Rec.	236-6
21M146, U (Ch. 401-21) Tel. Rec.	249-8
21M160, U (Ch. 406-21) Tel. Rec.	250-13
21M300 (Ch. 191, B) Tel. Rec.	201-5
21M305 (Ch. 201) Tel. Rec.	205-5
21M305B (Ch. 211, M) Tel. Rec.	194-4
21M308 (Ch. 196M, T) Tel. Rec.	195-8
21M314 (Ch. 211T) Tel. Rec. (See Model 21B122—Set 194-4)	
21M317, U (Ch. 300-21) Tel. Rec.	236-6
21M320, U (Ch. 401-21) Tel. Rec.	249-8
21M330, U (Ch. 406-21) Tel. Rec.	250-13
21M333, U (Ch. 406-21) Tel. Rec.	250-13
21M503 (Ch. 191, B) Tel. Rec.	201-5
21M506 (Ch. 211, M) Tel. Rec.	194-4
21M509 (Ch. 196) Tel. Rec. (See Model 21B116—Set 195-8)	
21M700 (Ch. 191, B) Tel. Rec.	201-5
21M700 (Ch. 196M, T) Tel. Rec.	195-8

HOFFMAN—Cont.

21M715 (Ch. 211T) Tel. Rec. (See Model 21B122—Set 194-4)	
21M718, U (Ch. 300-21) Tel. Rec.	236-6
21M721, U, 21M722, U (Ch. 400-21) Tel. Rec.	249-8
21M900 (Ch. 192) Tel. Rec. (TV Ch. only)	201-5
21M903 (Ch. 213, M) Tel. Rec.	211-8
21M906 (Ch. 199, M, T and Radio Ch. 182) Tel. Rec.	221-6
21P108 (Ch. 191, B) Tel. Rec.	201-5
21P117 (Ch. 196, M) Tel. Rec.	195-8
21P123 (Ch. 211, M) Tel. Rec.	194-4
21P145, U (Ch. 300-21) Tel. Rec.	236-6
21P148, U (Ch. 401-21) Tel. Rec.	249-8
21P307B (Ch. 211, M) Tel. Rec.	194-4
21P310 (Ch. 196M, T) Tel. Rec.	195-8
21P322, U (Ch. 400-21) Tel. Rec.	249-8
21P332, U (Ch. 405-21) Tel. Rec.	250-13
21P505 (Ch. 191, B) Tel. Rec.	201-5
21P508 (Ch. 211, M) Tel. Rec.	194-4
21P511 (Ch. 196) Tel. Rec. (See Model 21B116—Set 195-8)	
21P702 (Ch. 191, B) Tel. Rec.	201-5
21P702 (Ch. 196M, T) Tel. Rec.	195-8
21P717 (Ch. 211T) Tel. Rec. (See Model 21B122—Set 194-4)	
21P720, U (Ch. 300-21) Tel. Rec.	236-6
21P724, U (Ch. 400-21) Tel. Rec.	249-8
21P902 (Ch. 192) Tel. Rec. (TV Ch. only)	201-5
21P905 (Ch. 213, M) Tel. Rec.	211-8
21P908 (Ch. 199, M, T and Radio Ch. 182) Tel. Rec.	221-6
24B707 (Ch. 187, B, C) Tel. Rec.	159-6
24M708 (Ch. 187, B, C) Tel. Rec.	159-6
27M709 (Ch. 197) Tel. Rec.	219-6
600 (Ch. 154) Tel. Rec.	95A-8
601 (Ch. 155) Tel. Rec.	95A-8
610 (Ch. 140) Tel. Rec.	97A-6
612 (Ch. 142) Tel. Rec.	97A-6
613 (Ch. 149) Tel. Rec.	97A-6
630, 631 (Ch. 170) Tel. Rec.	150-7
632, 633, 634, 635 (Ch. 171) Tel. Rec.	150-7
634A, 635A (Ch. 173) Tel. Rec.	150-7
636, 637 (Ch. 183) Tel. Rec.	141-7
636B, 637B (Ch. 183 B) Tel. Rec.	141-7
638, 639 (Ch. 180) Tel. Rec.	144-5
826, 827, 828 (Ch. 143) Tel. Rec.	95A-8
830, 831 (Ch. 151) Tel. Rec.	93A-8
832 (Ch. 151) Tel. Rec. (See Model 830—Set 97A-6)	
836, 837 (Ch. 153) Tel. Rec.	93A-8
840 (Ch. 153) Tel. Rec.	93A-8
846 (Ch. 151) Tel. Rec. (See Model 830—Set 97A-6)	
847, 848, 849 (Ch. 156) Tel. Rec.	97A-7
860, 861, 862 (Ch. 157) Tel. Rec.	97A-7
866, A, 867, A, 868, A (Ch. 173) Tel. Rec.	150-7
870, 871, 872 (Ch. 170) Tel. Rec.	150-7
876, 877, 878 (Ch. 171) Tel. Rec.	150-7
876A, 877A, 878A (Ch. 173) Tel. Rec.	150-7
880, 881, 882, 883, 884, 885, 886, 887 (Ch. 183) Tel. Rec.	141-7
886B, 887B (Ch. 183B) Tel. Rec.	

MAJESTIC—Cont.

7P420 (Ch. 4705) 26-17
 7S433, 7S450, 7S470 (Ch. 4702, 4703) 22-19
 7YR752 (Ch. 7804A) 29-13
 7YR753 (Ch. 7809A-1), 7YR772 (Ch. 7809A) 42-17
 8FM744 (Ch. 8806D) 30-15
 8FM774 (Ch. 8808D), 8FM776 (Ch. 8807E) 30-15
 8ME89 (Ch. 8C07D) 29-14
 8J185 (Ch. 8L108) 47-12
 8S452, 8S473 (Ch. 4810) 8-19
 10FM89 (Ch. 10C23E) (See Model 10FM981—Set 65-8)
 12C4, 12C5 Tel. Rec. 108-7
 12FM475, 12FM778, 12FM779 (Ch. 4120) 28-20
 12FM893 (Ch. 12C22E) 59-11
 12T2, 12T3 Tel. Rec. 108-7
 12T6 Tel. Rec. (See Model 12C4—Set 138-7)
 14C4 Tel. Rec. (See Model 12C4—Set 138-7)
 14CT4 Tel. Rec. 133-8
 14T2 Tel. Rec. (See Model 12C4—Set 138-7)
 16C4, 16C5 Tel. Rec. 108-7
 16CT4, 16CT5 Tel. Rec. 133-8
 16T2, 16T3 Tel. Rec. 108-7
 17C42, 17C43 (Series 112, 112-2) Tel. Rec. (See Series 112—Set 233-4)
 17C62, 17C64, 17C65 (Series 106) Tel. Rec. (See PCB 43—Set 177-1 and Model 70—Set 153-8)
 17DA (Ch. 101) Tel. Rec. 127-7
 17GA, 17HA (Ch. 101) Tel. Rec. 127-7
 17TA61 17T681 (Series 106) Tel. Rec. (See Model 70—Set 153-8 and PCB 43—Set 177-1)
 17T40, 17C41 (Series 112, 112-2) Tel. Rec. (See Series 112—Set 233-4)
 17T62 (Series 106) Tel. Rec. (See Model 70—Set 153-8 and PCB 43—Set 177-1)
 19C4, 19C7 Tel. Rec. 133-8
 20C82, 20C83, 20C84 (Series 108) Tel. Rec. (See Model 70—Set 153-8 and PCB 43—Set 177-1)
 20F85, 20F86, 20F87 (Series 108) Tel. Rec. (See Model 70—Set 153-8 and PCB 43—Set 177-1)
 20F81 (Series 108) Tel. Rec. (See Model 70—Set 153-8 and PCB 43—Set 177-1)
 20T8A1 (Series 108) Tel. Rec. (See Model 70—Set 153-8 and PCB 43—Set 177-1)
 20T82, 20T83, 20T84 (Series 108) Tel. Rec. (See Model 70—Set 153-8 and PCB 43—Set 177-1)
 21C30, 21C31 (Series 108) Tel. Rec. (See Model 70—Set 153-8 and PCB 43—Set 177-1)
 21D40, 21D41 (Series 108) Tel. Rec. (See Model 70—Set 153-8 and PCB 43—Set 177-1)
 21D50, 21D51 (Series 108) Tel. Rec. (See Model 70—Set 153-8 and PCB 43—Set 177-1)
 21F86, 21F87 (Series 108) Tel. Rec. (See Model 70—Set 153-8 and PCB 43—Set 177-1)
 21F88, 21F89 (Series 108-5) Tel. Rec. (See Model 70—Set 153-8 and PCB 43—Set 177-1)
 21P62, 21P63 (Series 110, 111) Tel. Rec. 221-7
 21T20, 21T21 (Series 108) Tel. Rec. (See Model 70—Set 153-8 and PCB 43—Set 177-1)
 22 Thr. 35 (Series 106-5) Tel. Rec. (See Model 70—Set 153-8 and PCB 43—Set 177-1)
 70, 72, 73 (Series 106) Tel. Rec. (Also see PCB 43—Set 177-1)
 80FMP 137-6
 120, 121, 121B (Ch. 99) Tel. Rec. (Also see PCB 37—Set 166-2 and Model 17DA—Set 127-7)
 141, 41B (Ch. 100), 141C (Ch. 101), 142, 142B (Ch. 100) Tel. Rec. 127-7
 143 Tel. Rec. (See PCB 37—Set 166-2 and Model 17DA—Set 127-7)
 160, 160B, 162, 163 (Ch. 101) Tel. Rec. 127-7
 170 (Ch. 101) Tel. Rec. 127-7
 173 Tel. Rec. (See PCB 37—Set 166-2 and Model 17DA—Set 127-7)
 700, 701 (Series 106) Tel. Rec. (Also see PCB 43—Set 177-1)
 712, 715, 717, 718, 719 (Series 106) Tel. Rec. (Also see PCB 43—Set 177-1)
 800, 801, 802, 803, 804 (Series 108) Tel. Rec. (Also see PCB 43—Set 177-1)
 902, 903 (Ch. 103) Tel. Rec. 127-7
 910, 911 (Ch. 103) Tel. Rec. 127-7
 1042, G, GU, T, TX Tel. Rec. (See Model 12C4—Set 108-7)
 1043, G, GU, T, TX Tel. Rec. (See Model 12C4—Set 108-7)
 1142, 1143 Tel. Rec. (See Model 12C4—Set 108-7)
 1244, G, GU, T, TX Tel. Rec. (See Model 12C4—Set 108-7)
 1245, G, GU, T, TX Tel. Rec. (See Model 12C4—Set 108-7)
 1348 Tel. Rec. (See Model 12C4—Set 108-7)
 1400, B (Ch. 100) Tel. Rec. 127-7
 1401 (Ch. 105) Tel. Rec. (Also see PCB 37—Set 166-2) 127-7

MAJESTIC—Cont.

1546, G, GU, T, TX Tel. Rec. (See Model 12C4—Set 108-7)
 1547, G, GU, T, TX Tel. Rec. (See Model 12C4—Set 108-7)
 1548, G, GU, T, TX Tel. Rec. (See Model 12C4—Set 108-7)
 1549, G, GU, T, TX Tel. Rec. (See Model 12C4—Set 108-7)
 1600, 1600B (Ch. 101) Tel. Rec. 127-7
 1605, 1605B (Ch. 102) Tel. Rec. 127-7
 1610, 1610B (Ch. 102) Tel. Rec. 127-7
 1646, 1647, 1648, 1649 Tel. Rec. (See Model 12C4—Set 108-7)
 1671, 1672, 1673, 1674, 1675 Tel. Rec. 133-8
 1700C Tel. Rec. (See PCB 37—Set 166-2 and Model 17DA—Set 127-7)
 1710 (Ch. 101) Tel. Rec. 127-7
 1710C (Ch. 101) Tel. Rec. (See PCB 37—Set 166-2 and Model 17DA—Set 127-7)
 1720, 1721 Tel. Rec. (See PCB 37—Set 166-2 and Model 17DA—Set 127-7)
 1900 Tel. Rec. 95A-10
 1974, 1975 Tel. Rec. 133-8
 2042T, 2043T Tel. Rec. (See Model 12C4—Set 108-7)
 2546T, 2547T, 2549T Tel. Rec. (See Model 12C4—Set 108-7)
 Ch. 5B01A (See Model 5AK711)
 Ch. 5B05A (See Model 5AK731)
 Ch. 6B02D (See Model 6FM714)
 Ch. 6B11D (See Model 6FM773)
 Ch. 7B04A (See Model 7YR752)
 Ch. 7B09A (See Model 7YR772)
 Ch. 7B09B (See Model 7YR753)
 Ch. 7C11D (See Model 7FM837)
 Ch. 7C25A (See Model 7JL866)
 Ch. 8B06D (See Model 8FM744)
 Ch. 8B07D (See Model 8FM776)
 Ch. 8B08D (See Model 8FM775)
 Ch. 8C07D (See Model 8FM889)
 Ch. 10C23E (See Model 10FM891)
 Ch. 12B2AE (See Model 12FM475)
 Ch. 12C22E (See Model 12FM895)
 Ch. 18C90, 18C91 (See Model 17V850)
 Ch. 4501 (See Model 5A410)
 Ch. 4504 (See Model 5A300)
 Ch. 4506 (See Model 5A445)
 Ch. 4702, 4703 (See Model 7Y4333)
 Ch. 4705 (See Model 7P420)
 Ch. 4706 (See Model 7C432)
 Ch. 4707 (See Model 7C447)
 Ch. 4708 (See Model 7JK77R)
 Ch. 4810 (See Model 8S452)
 Ch. 4810B (See Model 8J185)
 Ch. 41201 (See Model 12FM475)
 Series 106 Tel. Rec. (See Model 70—Set 153-8)
 Series 106-5 Tel. Rec. (See PCB 43—Set 177-1 and Model 70—Set 153-8)
 Series 108, 108-5 Tel. Rec. (See PCB 43—Set 177-1 and Model 70—Set 153-8)
 Series 109 Tel. Rec. (See Model 70—Set 153-8)
 Series 110, 111 Tel. Rec. (See Model 21P62—Set 221-7)
 Series 112, 112-2, 113 Tel. Rec. 233-4

MASCO—Cont.

MA-17 14-32
 MA-17N 50-11
 MA-17P 14-32
 MA-17PN 50-11
 MA-20HF 28-21
 MA-25 16-24
 MA-25EX 60-15
 MA-25HF 54-13
 MA-25N 43-14
 MA-25NR 49-12
 MA-25P 52-24
 MA-25PN (See Model MA-25N—Set 43-14)
 MA-35 21-20
 MA-35N 44-11
 MA-35RC 21-20
 MA-30 30-16
 MA-50N (See Model MA-5NO—Set 45-15)
 MA-50NR 53-14
 MA-60 119-9
 MA-75 28-22
 MA-75N 52-27
 MA-77, MA-77R 19-7
 MA-121 24-21
 MA-125 188-8
 MA-808 26-18
 MAP-15 26-19
 MAP-18 59-12
 MAP-105 25-18
 MAP-105N 52-12
 MAP-120 21-21
 MAP-120N 46-15
 MA-50NR 196-5
 MB-50N 58-12
 MB-60 127-9
 MB-60 (Lute) 148-10
 MB-75 61-15
 MB-77 206-8
 MB-125 211-9
 MC-10 47-12
 MC-25, MC-25P 17-21
 MC-25N, MC-25PC, MC-25PN, MC-25RC 57-11
 MC-126, MC-126P 111-8
 MCR-5 15-18
 ME-8 152-10
 ME-18, ME-18P 151-8
 ME-27 155-21
 ME-36, ME-36R 154-7
 ME-52 149-7
 MHP-110 114-6
 MHP-110X 115-5
 Midgatelk 116-7
 MM-27P 153-9
 MPA-3, MPT-4 16-25
 MSD-16 150-9
 MU-5 117-6
 MU-17 185-8
 PR-1 218-6
 R-5 (Early) 33-11
 RK-5, RK-5L, RK-5M, RK-5AL, RK-4CZ 55L 168-11
 RK-55LR 177-9
 RK6, RK6R 244-7
 T-16 123-8
 TD-16 120-8
 TP-16A 30-17
 WF-1A 209-8
 76, 711 20-20
 86, 811 20-21

MECK—Cont.

JM720TU (Ch. 9021) Tel. Rec. 148-11
 JM721C, CD (Ch. 9032) Tel. Rec. 186-9
 JM721C, D (Ch. 9040) Tel. Rec. 220-4
 MM510T, MM512T, MM516C, MM-516T Tel. Rec. 110-9
 MM614C, T (Ch. 9018) Tel. Rec. (Also see PCB 12—Set 120-1)
 MM616C, T (Ch. 9018) Tel. Rec. (Also see PCB 12—Set 120-1)
 MM-617C, T (Ch. 9032) Tel. Rec. (See Model JM717C—Set 186-9)
 MM617T (Ch. 9040) Tel. Rec. 220-4
 MM619C (Ch. 9018) Tel. Rec. (Also see PCB 12—Set 120-1)
 MM-620C, T (Ch. 9032) Tel. Rec. (See Model JM717C—Set 186-9)
 MM621CPT, RPTB (Ch. 9040) Tel. Rec. 220-4
 MM621RPT, RPTB (Ch. 9040) Tel. Rec. 220-4
 M616C, T (Ch. 9023) Tel. Rec. (See Model JM717C—Set 148-11)
 M620T, T (Ch. 9023) Tel. Rec. (See Model JM717C—Set 148-11)
 PM-5CS-DW10 2-4
 MB-50N-PW10 12-19
 RC-5CS-P 1-9
 RC-6A7-P6 31-19
 SA-10, SA-20 10A-4
 XE-701 Tel. Rec. 61-16
 XA-705 (See Model XA-701—Set 61-16)
 XF-777 Tel. Rec. 101-5
 XL750 Tel. Rec. 76-14
 XM-752 Tel. Rec. 101-9
 XOB Tel. Rec. 110-9
 XP-775 Tel. Rec. 101-5
 XQA Tel. Rec. 110-9
 XQA-776 Tel. Rec. 101-5
 XQR Tel. Rec. 110-9
 XQ-777 Tel. Rec. 101-5
 XRA, XRT Tel. Rec. 110-9
 XR-778 Tel. Rec. 101-5
 XSA Tel. Rec. 110-9
 XSB (Ch. 9018) Tel. Rec. (Also see PCB 12—Set 120-1) 117-8
 XSC, XSD (Ch. 9018) Tel. Rec. (See Model MM514C—Set 117-8 and PCB 12—Set 120-1) 110-9
 XSPT Tel. Rec. 110-9
 XS-786 Tel. Rec. 101-5
 XTA, XTR Tel. Rec. 110-9
 XT-785 Tel. Rec. 101-5
 XX900 Tel. Rec. 110-9
 4CZ 35-14
 5A7-P11, 5A7-PB11 31-18
 5D7/WL18 21-22
 6A6-W4 16-26
 514C, T (Ch. 9018) Tel. Rec. (See Model MM614C—Set 117-8 and PCB 12—Set 120-1)
 614C, 614TL (Ch. 9022) Tel. Rec. (See Model JM717C—Set 148-11)
 616C, T (Ch. 9018) Tel. Rec. (See Model MM614C—Set 117-8 and PCB 12—Set 120-1)
 617C, 617TL (Ch. 9022) Tel. Rec. (See Model JM717C—Set 148-11)
 619C, T (Ch. 9018) Tel. Rec. (See Model MM614C—Set 117-8 and PCB 12—Set 120-1)
 9030 228-11
 Ch. 9018 (See Model MM614C)
 Ch. 9021 (See Model JM717C)
 Ch. 9022 (See Model 614C)
 Ch. 9023 (See Model M616T)
 Ch. 9032 (See Model JM717C)
 Ch. 9040 (See Model JM717C)

MERCURY (Pacific-Mercury)

2013 (Ch. 150-2) Tel. Rec. (Also see PCB 57—Set 190-1) 172-6
 2080 (Ch. 150-2) Tel. Rec. (See PCB 57—Set 190-1 and Model 2013—Set 172-6)
 2081 (Ch. 150-4 and Radio Ch. 155) Tel. Rec. 198-11
 2113, 2115 (Ch. 150-11, 81) Tel. Rec. (Also see PCB 57—Set 190-1) 172-6
 2116, 2117 (Ch. 150-81) Tel. Rec. (See PCB 57—Set 191-1 and Model 2013—Set 172-6)
 2181 (Ch. 150-31, 61 and Radio Ch. 155) Tel. Rec. 198-11
 2217, 2218, X (Ch. 200-11) Tel. Rec. 216-8
 2224 (Ch. 200-11) Tel. Rec. 216-8
 2284 (Ch. 200-11) Tel. Rec. 216-8
 2401 (Ch. 150-5, 51) Tel. Rec. (Also see PCB 57—Set 191-1)
 4120 (Ch. 150-2) Tel. Rec. (Also see PCB 57—Set 190-1) 172-6
 4222 (Ch. 150) Tel. Rec. (Also see PCB 57—Set 190-1) 172-6
 4317 (Ch. 150-9) Tel. Rec. 172-6
 4320 (Ch. 150-2, 15) Tel. Rec. (Also see PCB 57—Set 191-1)
 4421 (Ch. 150-81) Tel. Rec. (See Model 2013—Set 172-6 and PCB 57—Set 191-1)
 Ch. 150-2 (See Model 2013)
 Ch. 150-4 (See Model 2081)
 Ch. 150-5 (See Model 2401)
 Ch. 150-61 (See Model 2181)
 Ch. 150-81 (See Model 2131)
 Ch. 155 (See Model 2081)
 Ch. 200-11 (See Model 2217)

MIDLAND

M68 2-30

MIDWEST

P6, PB-6 14-19
 R-12, RG-12, RT-12 (Ch. RGT-12) 44-12
 R-12, RG-12, RT-12 (Ch. RGT-12) 44-13
 R-16, RG-16, RT-16 (Ch. RGT-16) 45-16
 SB, ST-8 (Ch. STM-8) 15-19
 S-12, SG-12, ST-12 (Ch. SGT-12) 21-23
 S-16, SG-16, ST-16 (Ch. SGT-16) 21-24
 TM-8 (Ch. STM-8) 15-19
 716, A (See Model S-16—Set 21-24)

MILWAUKEE ERWOOD (See Record Changer Listing)

MINERVA
 L702 12-20
 L725 11-15
 W-117, Tropic Master 6-17
 W-117-3 11-14
 W-702B 12-20
 W710, W710A (W119) 5-25
 W-728 11-15
 410, 111 30-8
 702H, 702H-1 30-8
 729 (Portugal) 23-14

MIRRORTONE (Also see Meck)
 A-17C, T (Ch. 9040) Tel. Rec. 216-4
 A-21C, CB, T, TB, X, Z (Ch. 9040) Tel. Rec. 216-4
 A24C (Ch. 9049, 9051) Tel. Rec. 247-6
 14MTS Tel. Rec. 163-7
 16MZ, 17MCM, MT, MZ, CZ, MZ-Tel. Rec. 163-7
 17PC (Ch. 9025) (Series "P") Tel. Rec. (See Model 20PC—Set 175-12)
 17PC58, 17PCW Tel. Rec. 204-5
 17PT (Ch. 9025) (Series "P") Tel. Rec. (See Model 20PC—Set 175-12)
 17PTE Tel. Rec. 204-5
 20MC, MT, MZ-C, MZ-Tel. Rec. 204-5
 21PCS Tel. Rec. 204-5
 21ODCS Tel. Rec. 204-5
 24QDCS (See Model A-17C) Tel. Rec. 251-11
 Ch. 9048 Tel. Rec. 250-14
 Ch. 9049 Tel. Rec. 247-6
 Ch. 9050 Tel. Rec. 250-14
 Ch. 9051 Tel. Rec. 247-6
 Ch. 9053, 9054 Tel. Rec. 250-14
 Ch. 9055 Tel. Rec. 251-11

MITCHELL
 T16-B, -M, T16-2KB, T16-2KM, T17-B, -M Tel. Rec. 154-8
 T172, T-172M Tel. Rec. 189-11
 T12-B, -M Tel. Rec. 190-9
 3D 251-12
 1200, 1251 55-14
 1252, 1253 155-12
 1254, 1255 159-8
 1256 156-8
 1257 158-7
 1268R 127-9
 1276, 1277 250-15

MOLDED INSULATION CO. (Also see Vix)
 MR-6 (Wiretone) 41-15

MONITOR—MOTOROLA

MONTGOMERY WARD

(See Airline)

602 (671A)	19-20
603	65-9
604	106-9
606	133-9
607	137-11
608	207-4
609	201-6
610T	220-5
611T (See Model 610T—Set 201-5)	
612 (See Model 609—Set 220-5)	
802 (C-4608)	18-24
802 (C-4608) (Revised)	42-19
803 (PD-4908)	66-12
804	67-12
805 (C-4908)	71-11
806, 807 (See Model 803—Set 66-12)	
808	107-6
809 (C-5009) (See Model 805—Set 71-11)	
810 (C-5010) (See Model 805—Set 71-11)	
812 (P-5106)	139-8
813 (D-5107)	139-8
814	137-7
815 (C-5109)	139-8
816 (C-5110)	139-8
817 (C-5111)	139-8
819 (P-5206)	202-3
820 (D-5207)	202-3
821	204-6
824 (C-5209)	202-3
828 (D-5407) (See Model 820—Set 202-3)	
829	247-7
830 (C-5409)	249-10

MONTGOMERY WARD

(See Airline)

MOPAR

602 (671A)	19-20
603	65-9
604	106-9
606	133-9
607	137-11
608	207-4
609	201-6
610T	220-5
611T (See Model 610T—Set 201-5)	
612 (See Model 609—Set 220-5)	
802 (C-4608)	18-24
802 (C-4608) (Revised)	42-19
803 (PD-4908)	66-12
804	67-12
805 (C-4908)	71-11
806, 807 (See Model 803—Set 66-12)	
808	107-6
809 (C-5009) (See Model 805—Set 71-11)	
810 (C-5010) (See Model 805—Set 71-11)	
812 (P-5106)	139-8
813 (D-5107)	139-8
814	137-7
815 (C-5109)	139-8
816 (C-5110)	139-8
817 (C-5111)	139-8
819 (P-5206)	202-3
820 (D-5207)	202-3
821	204-6
824 (C-5209)	202-3
828 (D-5407) (See Model 820—Set 202-3)	
829	247-7
830 (C-5409)	249-10

MOTOROLA (Also see Record Change Listing)

AR-96-23 (M-5)	11-16
BKO-A (See Ch. 10A—Set 106-10)	
BK2A (Ch. 2A and P6-2 or PB-2)	197-7
BK2M (Ch. 2M and P6-2 or PB-2)	197-7
BK-6	10-23
BK8, X (See Ch. 8A—Set 46-16)	
CR-6	20-24
CR-78	225-21
CTA3	230-7
CTO (See Model CT-9—Set 82-8)	
CT1 (See Ch. 1A—Set 134-8)	
CT1M	143-11
CT2A (Ch. 2A and P6-2 or PB-2)	197-7
CT2M (Ch. 2M and P6-2 or PB-2)	197-7
CT-6	8-21
CTB (See Ch. 8A—Set 46-16)	
CTB-A (See Ch. 10A—Set 106-10)	
CT-8	8-28
FD-6	7-20
FD7 (See Model FD-6—Set 7-20)	
FDB (See Ch. 8A—Set 46-16)	
GMOT (See Ch. 10A—Set 106-10)	
GMT2A (Ch. 2A and P6-2 or PB-2)	197-7
GMT2M (Ch. 2M and P6-2 or PB-2)	197-7
GM9T (See Ch. 8A—Set 46-16)	
GM9T-A (See Ch. 10A—Set 106-10)	
HJ2A (Ch. 2A and P6-2 or PB-2)	197-7
HJ2M (Ch. 2M and P6-2 or PB-2)	197-7
HNO (See Ch. 10A—Set 106-10)	
HN2A (Ch. 2A and P6-2 or PB-2)	197-7
HN2M (Ch. 2M and P6-2 or PB-2)	197-7
HNB, HN9 (See Ch. 8A—Set 46-16)	
HLTIC (See Ch. 10A—Set 106-10)	
HL2IC (See Ch. 1A—Set 134-8)	
HL2IZ (See Ch. 1A—Set 134-8)	
KR1 (See Ch. 1A—Set 134-8)	
KR2A (Ch. 2A and P6-2 or PB-2)	197-7
KR2M (Ch. 2M and P6-2 or PB-2)	197-7
KR8, KR9 (See Ch. 8A—Set 46-16)	
KR9A (See Ch. 10A—Set 106-10)	
NHIC	139-9
NH2AC (See Nash Model AC-152—Set 184-9)	
NH3C (See Nash Model NH3C—Set 216-6)	
NH6	9-24
NH8 (See Ch. 8A—Set 46-16)	
OEO (See Ch. 10A—Set 106-10)	
OE2 (See Ch. 8A—Set 46-16)	
OE2A (Ch. 2A and P6-2 or PB-2)	197-7
OE2M (Ch. 2M and P6-2 or PB-2)	197-7
OE6	8-21
OE8, OE9 (See Ch. 8A—Set 46-16)	
PCO (See Ch. 10A—Set 106-10)	
PC2 (See Ch. 8A—Set 46-16)	
PC2A (Ch. 2A and P6-2 or PB-2)	197-7
PC2M (Ch. 2M and P6-2 or PB-2)	197-7
PC6	8-21
PC8, PC9 (See Ch. 8A—Set 46-16)	
PC9-A (See Ch. 10A—Set 106-10)	
PD2A (Ch. 2A and P6-2 or PB-2)	197-7
PD2M (Ch. 2M and P6-2 or PB-2)	197-7

MOTOROLA—Cont.

SROB (Ch. OB)	103-7
SR18 (See Ch. 1B—Set 136-11)	
SR2A (Ch. 2A and P6-2 or PB-2)	197-7
SR2M (Ch. 2M and P6-2 or PB-2)	197-7
SR6, SR8, SR9 (See Ch. 8A—Set 46-16)	
SR9A (See Ch. 10A—Set 106-10)	
TC-101, B Tel. UHF Conv.	196-6
TK-17M Tel. UHF Conv.	193-5
TK19M Tel. UHF Conv.	193-5
TK19ME Tel. UHF Conv. (See Model TK17M—Set 193-5)	
TK-20M Tel. UHF Conv.	193-5
TK-22M Tel. UHF Conv.	193-5
TK-23M Tel. UHF Conv.	193-5
TK-24M Tel. UHF Conv.	193-5
TK-24ME Tel. UHF Conv. (See Model TK17M—Set 193-5)	
TK-31M Tel. UHF Conv. (See Model TK17M—Set 193-5)	
TK-33M Tel. UHF Conv. (See Model TK17M—Set 193-5)	
VF102, A, C (Ch. TS-7 and Radio Ch. HS-317) Tel. Rec.	51-14
VF103, VF103M (Ch. TS-8) Tel. Rec.	73-8
VK101, B, M (Ch. TS-5 and Radio Ch. HS-108) Tel. Rec.	51-14
VK106 (Ch. TS-9D) Tel. Rec. Photo-fact. Servicer	82
VK106, B, M (Ch. TS-9, A, B, C) Tel. Rec.	67-13
VK106, VK107 (Ch. TS-9E, TS-9E1) Tel. Rec.	77-6
VTK-17M, ME Tel. UHF Conv. (See Model TK17M—Set 193-5)	
VT71B, M-A (Ch. 4B through J) Tel. Rec.	55-16
VT-73, VT-73A (Chassis TS-4J Late) Tel. Rec.	71-12
VT101 (Ch. TS-3) Tel. Rec.	51-14
VT105 (Ch. TS-9D) Tel. Rec. Photo-fact. Servicer	82
VT105, VT105M (Ch. TS-9, TS-9A, TS-9B, TS-9C) Tel. Rec.	67-13
VT107 (Ch. TS-9D) Tel. Rec. Photo-fact. Servicer	82
VT107, B, M (Ch. TS-9, A, B, C) Tel. Rec.	67-13
VT121 (Ch. TS-15) Tel. Rec.	91A-9
WR6 (Ch. HS-18)	5-2
WR7, WR8 (See Model WR6—Set 5-2)	
WS1C (See Willys Model 677012—Set 156-14)	
WS2C (See Willys Model 679517—Set 172-12)	
Y17K17, B (Ch. TS-402Y) Tel. Rec.	237-8
Y17T15A, AE (Ch. VTS-402Y) Tel. Rec.	237-8
Y17T16, B (Ch. TS-402Y) Tel. Rec.	237-8
Y21C2, B (Ch. TS-502Y) Tel. Rec.	237-8
Y21F5, B (Ch. TS-502Y and Radio Ch. HS-409) Tel. Rec. (TV Chassis only)	237-8
Y21K12A, AB, WA (Ch. WTS-502Y) Tel. Rec.	237-8
Y21K13, B, Y21K14, B, Y21K15, Y21K16, W, Y21K17 (Ch. TS-502Y) Tel. Rec.	237-8
Y21T8A, AE (Ch. TTS-502Y) Tel. Rec.	237-8
Y21T11, B, W (Ch. VTS-502Y) Tel. Rec.	237-8
Y24K1, B, Y24K2, B, Y24K3, W (Ch. TS-602Y) Tel. Rec.	233-6
Y27K2, B, Y27K3 (Ch. TS-602Y) Tel. Rec.	233-6
2MF (See Ford Model 2MF—Set 175-10)	
3MF (See Ford Model 3MF—Set 206-51)	
3MFT (See Ford Model 3MFT—Set 215-7)	
5A1 (Ch. HS-6)	2-11
5A5 (Ch. HS-15)	3-11
5A7 (Ch. HS-62), 5A7A (Ch. HS-62A)	29-16
5C1 (Ch. HS-228)	116-9
5C2 (Ch. HS-258)	116-9
5C3 (Ch. HS-262)	116-9
5C4 (Ch. HS-270)	116-9
5C5 (Ch. HS-271) (See Model 5C1—Set 116-9)	
5C6 (Ch. HS-272) (See Model 5C1—Set 116-9)	
5H11U, 5H12U, 5H13U (Ch. HS-224)	117-9
5J1 (Ch. HS-250), 5J1U (Ch. HS-224)	100-7
5J2 (Ch. HS-250) (See Model 5J1—Set 100-7)	
5J2U (Ch. HS-224) (See Model 5J1—Set 100-7)	
5L1 (Ch. HS-250), 5L1U (Ch. HS-224)	100-7
5L2 (Ch. HS-250) (See Model 5J1—Set 100-7)	
5L2U (Ch. HS-224) (See Model 5J1—Set 100-7)	
5M1, 5M2, 5M2Z, 5M2U (Ch. HS-249, HS-223)	101-7
5R11A, 5R12A, 5R13A, 5R14A, 5R15A, 5R16A (Ch. HS-280) (See Model 5R11U—Set 115-6)	
5R11U, 5R12U, 5R13U, 5R14U, 5R15U, 5R16U (Ch. HS-242)	115-6
5X11U, 5X12U, 5X13U (Ch. HS-243)	114-7
5X21U, 5X22U, 5X23U (Ch. HS-259)	120-9
6F11, F11B (Ch. HS-264)	117-10
6L1, 6L2 (Ch. HS-226)	102-7
6X11U, 6X12U (Ch. HS-245)	112-5
7F11, 7F11B (Ch. HS-265)	113-5
7VT1, 7VT2, 7VTS (Ch. TS-18) Tel. Rec.	83-6
8FDT (See Ch. 8A—Set 46-16)	
8FM21, 8FM21B (Ch. HS-247)	121-9
8GMT (See Ch. 8A—Set 46-16)	

MOTOROLA—Cont.

9FM21, 9FM21B (Ch. HS-246)	114-8
9T1 (Ch. TS-18, A) Tel. Rec. (See Model 9T11—Set 83-6)	
9V11, 9VTS (Ch. TS-18, A) Tel. Rec.	83-6
10T2 (Ch. TS-14B) Tel. Rec.	92-4
10V9K (Ch. TS-9E, TS-9E1) Tel. Rec.	77-6
10VX12 (Ch. TS14, A, B) Tel. Rec.	92-4
10VX22 (Ch. TS14, A, B) Tel. Rec.	92-4
10VX4 (Ch. TS-9E, TS-9E1) Tel. Rec.	77-6
10VX13 (Ch. TS-9E, TS-9E1) Tel. Rec.	77-6
10VX10 (Ch. TS14, A, B) Tel. Rec.	92-4
10VX24 (Ch. TS14, A, B) Tel. Rec.	92-4
12K1, B (Ch. TS23B) Tel. Rec.	92-4
12K1, B (Ch. TS-53) Tel. Rec. (See Model 12K2—Set 115-7)	
12K2, B (Ch. TS-53) Tel. Rec.	115-7
12K2, B (Ch. TS-53) Tel. Rec.	115-7
12K3, B (Ch. TS-53) Tel. Rec. (See Model 12K3—Set 115-7)	
12T1, B (Ch. TS-23B) Tel. Rec.	92-4
12T1, B (Ch. TS-23B) Tel. Rec.	92-4
12T1, B, 12T2, B (Ch. TS-53) Tel. Rec. (See Model 12T3—Set 115-7)	
12T3 (Ch. TS-53) Tel. Rec.	115-7
12VF4B, R, R.C (Ch. TS-23, A and Radio Ch. HS-190) Tel. Rec.	92-4
12VF24B, B, R, R.C (Ch. TS-23, A and Radio Ch. HS-190A) Tel. Rec.	92-4
12VK11 (Ch. TS-23, A, B) Tel. Rec.	92-4
12VK15 (Ch. TS-30, A) Tel. Rec. (Also PCB 52-126-1)	93-2
12VK18B, 12VK18R (Ch. TS-15C, TS-15C1) Tel. Rec.	77-6
12VT13 (Ch. TS-23, A, B) Tel. Rec.	92-4
12VT16, 12VT16B, 12VT16R (Ch. TS-15C, TS-15C1) Tel. Rec.	77-6
14K1, B (Ch. TS-88) Tel. Rec.	112-6
14K18H, 14K18H (Ch. TS-115) Tel. Rec.	121-10
14P18 (Ch. TS-216) Tel. Rec. (See Model 14T4—Set 158-8)	
14P21, 14P2U (Ch. TS-275) Tel. Rec.	174-9
14T1, B (Ch. TS-88) Tel. Rec.	112-6
14T3 (Ch. TS-114) Tel. Rec.	121-10
14T3X1 (Ch. TS-114A) (See Model 14T3—Set 121-10)	
14T4, B (Ch. TS-216) Tel. Rec.	158-8
16F1 (Ch. TS-60 and Radio Ch. HS-23) Tel. Rec.	102-8
16F1B, 16F1H (Ch. TS-89 and Radio Ch. HS-324) Tel. Rec. (For TV Ch. see Set 121-10, for Radio Ch. see Model 16F1—Set 102-8)	
16K2L, L-B (Ch. TS-52) Tel. Rec.	93A-10
16K7 (Ch. TS-74) Tel. Rec.	102-8
16K28H, 16K28H (Ch. TS-94) Tel. Rec.	121-10
16T1 (Ch. TS-60) Tel. Rec.	102-8
16T18H, 16T18H (Ch. TS-89) Tel. Rec.	121-10
16VFB8, R (Ch. TS-16, A and Radio Ch. HS-317) Tel. Rec. (For TV Ch. see Set 93-7, for Radio Ch. see Model 9FM21—Set 80-10)	
16VK1 (Ch. TS-52) Tel. Rec.	93A-10
16VK7 (Ch. TS-16, A) Tel. Rec. (Also PCB 52-106-1)	93-2
17F1 (Ch. TS-118 and Radio Ch. HS-253) Tel. Rec.	121-10
17F1A (Ch. TS-89 and Radio Ch. HS-253) Tel. Rec.	121-10
17F1B (Ch. TS-118 and Radio Ch. HS-253) Tel. Rec.	121-10
17F1BA (Ch. TS-89 and Radio Ch. HS-253) Tel. Rec.	121-10
17F2W (Ch. TS-118 and Radio Ch. HS-253) Tel. Rec.	121-10
17F2W (Ch. TS-89 and Radio Ch. HS-253) Tel. Rec.	121-10
17F3, B (Ch. TS-118 and Radio Ch. HS-253) Tel. Rec.	121-10
17F3BA (Ch. TS-89 and Radio Ch. HS-253) Tel. Rec.	121-10
17F3C (Ch. TS-118 and Radio Ch. HS-253) Tel. Rec. (See Model 14K18H)	121-10
17F4A (Ch. TS-89 and Radio Ch. HS-253) Tel. Rec.	121-10
17F5 (Ch. TS-118 and Radio Ch. HS-261) Tel. Rec. (See Model 14K18H)	121-10
17F5A, 17F5BA (Ch. TS-89 and Radio Ch. HS-261) Tel. Rec.	121-10
17F5B (Ch. TS-118 and Radio Ch. HS-261) Tel. Rec.	121-10
17F6, B (Ch. TS-118 and Radio Ch. HS-253) Tel. Rec. (See Model 14K18H—Set 121-10)	
17F6B, C (Ch. TS-174 and Radio Ch. HS-253) Tel. Rec. (See Model 14K18H—Set 121-10)	
17F7B (Ch. TS-118) Tel. Rec. (See Model 14K18H—Set 121-10)	
17F7BC (Ch. TS-174 and Radio Ch. HS-253) Tel. Rec. (See Model 14K18H—Set 121-10)	
17F7C (Ch. TS-118) Tel. Rec. (See Model 14K18H—Set 121-10)	
17F7D (Ch. TS-118) Tel. Rec. (See Model 14K18H—Set 121-10)	
17F7E, F (Ch. TS-314A, B, TS-316A, B) Tel. Rec.	167-13
17F7B, C, D (Ch. TS-236) Tel. Rec.	152-4A
17F7BF, F (Ch. TS-228) Tel. Rec.	165-7
17T6G (Ch. TS-314A, B) Tel. Rec.	167-13
17T7, A (Ch. TS-325, TS-326) Tel. Rec.	171-8
17T8, A, B, BA (Ch. TS-325, TS-326, A, and Radio Ch. HS-319) Tel. Rec.	171-8
17T9E (Ch. TS-401) Tel. Rec. (For TV Ch. only see PCB 49—Set 183-1 and Model 21F1—Set 173-9)	
17F13, B (Ch. TS-395A, 02 and Radio Ch. HS-319) (For TV Ch. see Set 192-6, for Radio Ch. see Model 17F12—Set 171-8)	
17F13BC (Ch. TS-408A and Radio Ch. HS-319) Tel. Rec. (See Model 21C1—Set 191-13, for Radio Ch. see Model 17F12—Set 171-8)	
17F13C (Ch. TS-408A and Radio Ch. HS-319) Tel. Rec. (For TV Ch. only see PCB 49—Set 183-1 and Model 21F1—Set 173-9)	
17T10 (Ch. TS-395A, 02 and Model 21C1—Set 191-13)	
17T10A (Ch. TS-326A, B) Tel. Rec. (See Model 17F12—Set 171-8)	
17T10D (Ch. TS-401) Tel. Rec. (See PCB 49—Set 183-1 and Model 21F1—Set 173-9)	
17T11 (Ch. TS-395, 02) Tel. Rec.	192-6
17T11C (Ch. TS-408A) Tel. Rec. (See Model 21C1—Set 191-13)	
17T11E (Ch. TS-400A) Tel. Rec.	194-9
17T11EC (Ch. TS-408A) Tel. Rec. (See Model 21C1—Set 191-13)	
17T12, B (Ch. TS-395A, 02) Tel. Rec.	192-6
17T12C (Ch. TS-408A) Tel. Rec. (See Model 21C1—Set 191-13)	
17T12W (Ch. TS-395A, 02) Tel. Rec.	192-6
17T12WC (Ch. TS-408A) Tel. Rec. (See Model 21C1—Set 191-13)	
17T13 (Ch. TS-410A) Tel. Rec. (Also see PCB 76—Set 217-1)	
17T13Y (Ch. TS-410Y) Tel. Rec. (See PCB 76—Set 217-1 and Model 17T13—Set 194-9)	
17T14 (Ch. VTS-410A) Tel. Rec. (See PCB 76—Set 217-1 and Model 17T13—Set 194-9)	
17T14Y (Ch. VTS-410Y) Tel. Rec. (See PCB 76—Set 217-1 and Model 17T13—Set 194-9)	
17T15, A, E (Ch. VTS-402) Tel. Rec.	237-8
17T16, B, AE (Ch. TS-228) Tel. Rec.	171-8
19F1 (Ch. TS-67, A and Radio Ch. HS-230) Tel. Rec.	111-9
19K1 (Ch. TS-67, A) Tel. Rec.	111-9
19K2, 19K2B (Ch. TS-101) Tel. Rec.	122-5
19K2E, BE (Ch. TS-119, A) Tel. Rec. (See PCB 53—Set 187-1 and Model 19K2—Set 122-5)	
19K3, 19K4, 19K4B (Ch. TS-101) Tel. Rec.	122-5
20F1, B (Ch. TS-119, A and Radio Ch. HS-230) Tel. Rec. (Also see PCB 53—Set 187-1)	
20F2, B (Ch. TS-119B, C) Tel. Rec. (See PCB 53—Set 187-1 and Model 19K2—Set 122-5)	
20K1, B, 20K2 (Ch. TS-119B, C) Tel. Rec. (See PCB 53—Set 187-1 and Model 19K2—Set 122-5)	
20K3, B, 20K4, B (Ch. TS-119B, C) Tel. Rec. (See PCB 53—Set 187-1 and Model 19K2—Set 122-5)	
20K6, 20K6B (Ch	

MOTOROLA—Cont.

21F3Y (Ch. TS-292A), BY, CY and Radio Ch. HS-216A) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 198-13)
21F5, B Ch. TS-502 and Radio Ch. HS-40F) Tel. Rec. (TV chassis only) 237-8
21K1, B (Ch. TS-351) Tel. Rec. 173-9
21K2, B (Ch. TS-351) Tel. Rec. 173-9
21K3, B, W (Ch. TS-351B) Tel. Rec. (See Model 21F1—Set 173-9)
21K4, A (Ch. TS-292A, B, C) Tel. Rec. (Also see PCB 63—Set 197-1 and PCB 73—Set 214-1) 191-13
21K4AY (Ch. TS-292AY, BY, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21K4B (Ch. TS-292A, B, C) Tel. Rec. (Also see PCB 63—Set 197-1 and PCB 73—Set 214-1) 191-13
21K4BD, BDY (Ch. WTS-292A, AY, B, BY, C, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21K4BY (Ch. TS-292AY, BY, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21K4C, CB, CBY, CW, CWY, CY, D, DY (Ch. WTS-292A, AY, B, BY, C, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21K4W (Ch. TS-292A, B, C) Tel. Rec. (Also see PCB 63—Set 197-1 and PCB 73—Set 214-1) 191-13
21K4WD, WDY (Ch. WTS-292A, AY, B, BY, C, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21K4WY, 21K4Y (Ch. TS-292AY, BY, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21K5, E (Ch. TS-292A, B, C) Tel. Rec. (Also see PCB 63—Set 197-1 and PCB 73—Set 214-1) 191-13
21K5BD, BDY (Ch. WTS-292A, AY, B, BY, C, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21K5BY (Ch. TS-292AY, BY, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21K5D, DY (WTS-292A, AY, B, BY, C, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21K5Y (Ch. TS-292AY, BY, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21K6 (Ch. TS-292A, B, C) Tel. Rec. (Also see PCB 63—Set 197-1 and PCB 73—Set 214-1) 191-13
21K6D, DY (Ch. WTS-292A, AY, B, BY, C, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21K6Y (Ch. TS-292AY, BY, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21K7 (Ch. TS-292A, B, C) Tel. Rec. (Also see PCB 63—Set 197-1 and PCB 73—Set 214-1) 191-13
21K7D, DY (Ch. WTS-292A, AY, B, BY, C, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21K7Y (Ch. TS-292AY, BY, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21K9, Y (Ch. WTS-292A, AY, B, BY, C, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21K10, B, BY, C (Ch. TS-292A, AY, B, BY, C, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21K11, B, BY, C (Ch. VTS-292A, AY, B, BY, C, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21K12A, AB, WA (Ch. WTS-502) Tel. Rec. 237-8
21K13, B, 21K14, B, 21K15, 21K16, W, 21K17 (Ch. TS-502) Tel. Rec. 237-8
21T1, B (Ch. TS-351) Tel. Rec. 173-9
21T2, B (Ch. TS-351) Tel. Rec. 173-9
21T3 (Ch. TS-501A, B) Tel. Rec. (Also see PCB 63—Set 197-1) 191-13
21T4A (Ch. TS-324A, B) Tel. Rec. (Also see PCB 63—Set 197-1) 191-13
21T4AC, ACE (Ch. TS-292B, C) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21T4ACY (Ch. TS-292AY, BY, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21T4EA (Ch. TS-324A, B) Tel. Rec. (Also see PCB 63—Set 197-1) 191-13
21T5A, BA (Ch. TS-324A, B) Tel. Rec. (Also see PCB 63—Set 197-1) 191-13

MOTOROLA—Cont.

21T7, B, BY, Y (Ch. VTS-292A, AY, B, BY, C, CY) Tel. Rec. (See PCB 63—Set 197-1, PCB 73—Set 214-1 and Model 21C1—Set 191-13)
21T8A, AE (Ch. TS-502) Tel. Rec. 237-8
21T11, B, W (Ch. VTS-502) Tel. Rec. 237-8
21K1, B, 24K2, B, 24K3, W (Ch. TS-602) Tel. Rec. 233-6
27K2, B, 27K3 (Ch. TS-602) Tel. Rec. 233-6
42B1 (Ch. HS-306) 191-14
45B12 (Ch. HS-8) 9-23
47B11 (Ch. HS-72) 29-17
48L11 (Ch. HS-113) 47-13
49L11Q, 49L13Q (Ch. HS-183) 77-7
51C1, 51C2, 51C3, 51C4 (Ch. HS-288) (See Model 5C1—Set 115-9)
51L11 (Ch. HS-309) (See Model 5J1—Set 100-7)
51M1U, 51M2U (Ch. HS-283) 149-8
52B1U (Ch. HS-305) 190-10
52C1 (Ch. HS-309) 191-15
52C1A (Ch. HS-309) (See Model 5C1—Set 191-15)
52C2 (Ch. HS-310) 177-10
52C6A (Ch. HS-375) (See Model 52C6—Set 177-10)
52C7 (Ch. HS-310) 177-10
52C7A (Ch. HS-310) (See Model 52C7—Set 177-10)
52C8 (Ch. HS-310) 177-10
52C8A (Ch. HS-375) (See Model 52C8—Set 177-10)
52CW1, 52CW2, 52CW3, 52CW4 (Ch. HS-329) 190-10
52H1U, 52H12U, 52H13U, 52H14U (Ch. HS-313) 176-6
52L1, A, 52L2, A, 52L3, A (Ch. HS-327, HS-357) 190-11
52M1U, 52M2U, 52M3U (Ch. HS-300) 188-10
52R1, 52R2, 52R3, 52R4, 52R5, 52R16 (Ch. HS-289) 188-11
52R11, 52R12, 52R13, 52R14, 52R15, 52R16 (Ch. HS-289A) (See Model 52R11—Set 188-11)
52R11A, 52R12A, 52R13A, 52R14A, 52R15A, 52R16A (Ch. HS-317) 178-7
52R11U, 52R12U, 52R13U, 52R14U, 52R15U, 52R16U (Ch. HS-315) 177-11
53C1, 53C2, 53C3, 53C4 (Ch. HS-366) 235-6
53C6, 53C7, 53C8, 53C9 (Ch. HS-338) 235-7
53F2 (Ch. HS-360) 234-9
53H1, 53H2, 53H3, 53H4 (Ch. HS-337) 250-16
53LC1, 53LC2, 53LC3 (Ch. HS-139) 217-10
53R1, U, 53R2, U, 53R3, U, 53R4, U, 53R5, U, 53R6, U (Ch. HS-384, HS-426) 247-8
53X1, 53X2, 53X3, 53X4 (Ch. HS-336) 236-8
53Y1 (Ch. HS-30) 24-11
55X11A, 55X12A, 55X13A, 2-22
56X11 (Ch. HS-94) 28-24
57X11, 57X12 (Ch. HS-60) 28-25
58A11, 58A12 (Ch. HS-158) 52-13
58G11, 58G12 (Ch. HS-160) 64-8
58L11 (Ch. HS-114) 65-17
58R11, 58R12, 58R13, 58R14, 58R15, 58R16 (Ch. HS-116) 49-14
58R11A, 58R12A, 58R13A, 58R14A, 58R15A, 58R16A (Ch. HS-184) 69-11
58X11, 58X12 (Ch. HS-125) 53-10
59F11 (Ch. HS-188) 68-12
59H11U, 59H12U (Ch. HS-210) 97-9
59L11Q, 59L12Q, 59L14Q (Ch. HS-187) 78-10
59R11, 59R12, 59R13, 59R14E, 59R15C, 59R16Y (Ch. HS-167) 79-10
59X11, 59X12 (Ch. HS-180) 41-11
59X21U, 59X221U (Ch. HS-192) 98-26
61L1, 61L2 (Ch. HS-226) (See Model 61L1—Set 102-7)
62C1 (Ch. HS-299) 189-12
62C1A (Ch. HS-299) (See Model 62C1—Set 189-12)
62C2 (Ch. HS-299) 189-12
62C2A (Ch. HS-299) (See Model 62C2—Set 189-12)
62C3 (Ch. HS-299) 189-12
62C3A (Ch. HS-299) (See Model 62C3—Set 189-12)
62CW1 (Ch. HS-324) 196-7
62L1U, 62L2U, 62L3U (Ch. HS-208) 183-10
62X11U, 62X12U, 62X13U (Ch. HS-314) 175-14
62X21 (Ch. HS-326) 228-12
63L5S (Ch. HS-415) 251-13
63L1, 63L2, 63L3 (Ch. HS-161) 22-8
63X1, 63X1A, 63X2, 63X3 (Ch. HS-335) 238-9
63X21 (Ch. HS-385) 249-11
65F11 (Ch. HS-31) 6-19
65F12 (See Model 65F11—Set 6-19)
65L1, 65L2 (Ch. HS-7) 8-22
65L11, 65L12 (Ch. HS-7) 8-22
65T21, 65T21B (Ch. HS-32) 1-1
65X11A, 65X12A, 65X13A, 65X14A, 65X14B (Ch. HS-2) 4-8
67F11, 67F12, 67F12B (Ch. HS-63) 31-20
67F14 (Ch. HS-122) 55-15
67F61BN (Ch. HS-69) 44-14
67L11 (Ch. HS-59) 31-21
67X11, 67X12, 67X13 (Ch. HS-58) 30-20
67XM21 (Ch. HS-64) 32-14
68F11, 68F12, 68F14, 68F14B, 68F14M 58-13
68L11 (Ch. HS-119) 45-18
68T11 (Ch. HS-144) 45-14

MOTOROLA—Cont.

68X11, 68X12 (Ch. HS-127), 68X11A, 68X12A (Ch. HS-27A) 56-16
69L11 (Ch. HS-175) 76-15
69X11, 69X121 (Ch. HS-181) 82-9
72XM21 (Ch. HS-303) 176-7
72XM22 (See Model 72XM21—Set 176-7)
75F21 (Ch. HS-91) 19-21
75F31 (Ch. HS-36), 75F31A, B (Ch. HS-36A), 76F31 (Ch. HS-98) 29-18
77FM21 (Ch. HS-89), 77FM22, 77FM22M, 77FM22WM, 77FM23 (Ch. HS-97) 33-13
77XM21, 77XM22, 77XM22B (Ch. HS-102) 34-12
78F11, 78F11M (Ch. HS-150), 78F12M (Ch. HS-155) 56-17
78FM21, 78FM21M (Ch. HS-132), 78FM22 (Ch. HS-128), 59-13
79FM21, 79FM21B, 78FM21R (Ch. HS-178) 88-7
79XM21, 79XM22 (Ch. HS-168) 85-9
85F21 (Ch. HS-22) 6-20
85K21 (Ch. HS-52) 5-3
88FM21 (Ch. HS-133) 54-15
91FM21 (Ch. HS-230A) (See Model 19F1—Set 111-9)
92FM21, A, B, BA (Ch. HS-316A) (See Model 21F1—Set 173-9)
95F31, 95F31B (Ch. HS-39) 95F33 (Ch. HS-38) 19-22
99FM21R (Ch. HS-170) 80-10
107F31, 107F31B (Ch. HS-87) 33-14
309 63-14
400 99-10
401 131-12
401A 179-8
403 216-5
405 (Ch. AS-13) 3-8
405M (See Set 21-25 and Model 405—Set 3-8) 38-12
409 (See Model 408—Set 38-12) 215-10
500 98-7
501 133-10
501A 148-12
502 22-8
505 (Ch. AS-14) 4-37
508 39-13
509 (See Model 508—Set 39-13) 553
600 97-10
600 (See Mopar Model 603—Set 65-9)
604 (See Mopar Model 704—Set 106-9)
605 (Ch. AS-15) 5-1
606 (See Mopar Model 606—Set 133-9)
607 (See Mopar Model 607—Set 170-11)
608 39-14
608 (Mopar) (See Mopar Model 608—Set 207-4)
609 (See Model 608—Set 39-14)
611 (See Mopar Model 610T—Set 220-5)
612 (See Mopar Model 609—Set 201-6)
700 100-8
701 137-8
702 (Ch. BT-2 and 6-2) 197-7
703 (Ch. AS-16) 7-19
708 40-12
709 (See Model 708—Set 40-12) 800 103-10
802 (Ch. BT-2 and P8-2) 138-6
804 (See Mopar Model 804—Set 67-12)
808 (See Mopar Model 808—Set 107-6)
814 (See Mopar Model 814—Set 137-8)
829 (See Mopar Model 829—Set 247-7)
Ch. AS-13 (See Model 405)
Ch. AS-15 (See Model 605)
Ch. AS-16 (See Model 703)
Ch. AS-22 (See Model BK-6)
Ch. BT-2 197-7
Ch. HS-2 (See Model 65X11A)
Ch. HS-6 (See Model 5A1)
Ch. HS-7 (See Model 65L11)
Ch. HS-8 (See Model 45B12)
Ch. HS-15 (See Model 5A5)
Ch. HS-18 (See Model WR6)
Ch. HS-22 (See Model 85F21)
Ch. HS-26 (See Model 65F21)
Ch. HS-30 (See Model 55F11)
Ch. HS-31 (See Model 65F11)
Ch. HS-32 (See Model 65T21)
Ch. HS-36 (See Model 75F31)
Ch. HS-36A (See Model 75F31A)
Ch. HS-38 (See Model 95F33)
Ch. HS-39 (See Model 95F31)
Ch. HS-42 (See Model 67X11)
Ch. HS-52 (See Model 85K21)
Ch. HS-58 (See Model 67X11)
Ch. HS-59 (See Model 67L11)
Ch. HS-60 (See Model 57X11)
Ch. HS-62 (See Model 5A7)
Ch. HS-62A (See Model 5A7A)
Ch. HS-63 (See Model 67F11)
Ch. HS-64 (See Model 67XM21)
Ch. HS-69 (See Model 67F61BN)
Ch. HS-72 (See Model 47B11)
Ch. HS-87 (See Model 107F31)
Ch. HS-89 (See Model 77FM21)
Ch. HS-91 (See Model 75F21)
Ch. HS-94 (See Model 56X11)
Ch. HS-97 (See Model 77FM22)
Ch. HS-98 (See Model 76F31)
Ch. HS-99 (See Model 75X11)
Ch. HS-108 (See Model VK-101)
Ch. HS-113 (See Model 48L11)
Ch. HS-114 (See Model 58L11)
Ch. HS-116 (See Model 58R11)
Ch. HS-119 (See Model 68L11)
Ch. HS-122 (See Model 67F14)
Ch. HS-124 (See Model 78F11)
Ch. HS-125 (See Model 58X11)

MOTOROLA—Cont.

Ch. HS-127 (See Model 68X11)
Ch. HS-127A (See Model 68X11A)
Ch. HS-128 (See Model 78FM22M)
Ch. HS-132 (See Model 78FM21)
Ch. HS-133 (See Model 88FM21)
Ch. HS-137 (See Model VF102)
Ch. HS-144 (See Model 68T11)
Ch. HS-150 (See Model 67L11)
Ch. HS-155 (See Model 78F12M)
Ch. HS-158 (See Model 58A11)
Ch. HS-160 (See Model 58G11)
Ch. HS-167 (See Model 59R11)
Ch. HS-168 (See Model 79XM21)
Ch. HS-170 (See Model 99FM21R)
Ch. HS-175 (See Model 69L11)
Ch. HS-178 (See Model 79FM21)
Ch. HS-180 (See Model 59X11)
Ch. HS-181 (See Model 69X11)
Ch. HS-183 (See Model 49L11Q)
Ch. HS-184 (See Model 58R11A)
Ch. HS-187 (See Model 59L11U)
Ch. HS-188 (See Model 59F11)
Ch. HS-192 (See Model 59X21U)
Ch. HS-210 (See Model 59H11U)
Ch. HS-223 (See Model 5M1)
Ch. HS-224 (See Model 5J1U)
Ch. HS-226 (See Model 611)
Ch. HS-228 (See Model 5C1)
Ch. HS-230 (See Model 19F1)
Ch. HS-234 (See Model 16F1)
Ch. HS-242 (See Model 5R11U)
Ch. HS-243 (See Model 5X11U)
Ch. HS-244 (See Model 5H11U)
Ch. HS-245 (See Model 5C2)
Ch. HS-246 (See Model 9FM21)
Ch. HS-247 (See Model 8FM21)
Ch. HS-249 (See Model 5M1)
Ch. HS-250 (See Model 5J1)
Ch. HS-253 (See Model 17F1)
Ch. HS-258 (See Model 5C2)
Ch. HS-259 (See Model 5X21U)
Ch. HS-261 (See Model 17F5)
Ch. HS-262 (See Model 5C3)
Ch. HS-264 (See Model 6F11)
Ch. HS-265 (See Model 7F11)
Ch. HS-270 (See Model 5C2)
Ch. HS-271 (See Model 5C5)
Ch. HS-272 (See Model 5C6)
Ch. HS-283 (See Model 51M1U)
Ch. HS-289, A (See Model 52R11)
Ch. HS-299 (See Model 62C1)
Ch. HS-300 (See Model 52M1U)
Ch. HS-337 (See Model 52R11)
Ch. HS-338 (See Model 53C6)
Ch. HS-347 (See Model 53C1C)
Ch. HS-357 (See Model 52L1)
Ch. HS-360 (See Model 53F2)
Ch. HS-361 (See Model 63L1)
Ch. HS-374 (See Model 53C1)
Ch. HS-384 (See Model 53R1)
Ch. HS-385 (See Model 63X21)
Ch. HS-415 (See Model 63L5S)
Ch. HS-426 (See Model 53R1U)
Ch. A-5 (See Model AR9-23)
Ch. OB (See Model SR0B)
Ch. P6-2 197-7
Ch. P8-2 197-7
Ch. TS-3 (See Model VT-101)
Ch. TS-4B Thru J (See Model VT-71)
Ch. TS-4J Late (See Model VT-73)
Ch. TS-5 (See Model 58L11)
Ch. TS-7 (See Model VF-102)
Ch. TS-8 (See Model VF103)
Ch. TS-9, TS-9A, TS-9B, TS-9C (See Model VT105)
Ch. TS-9D (See Model VT105)
Ch. TS-9E, TS-9E1 (See Model VK106)
Ch. TS-14, A, B (See Model 10VK-12)
Ch. TS-15 (See Model VT121)
Ch. TS-15C, TS-15C1 (See Model 12VK18B)
Ch. TS-16, A (See Model 16VF8B)
Ch. TS-18, A (See Model 7VT1)
Ch. TS-23, A, B (See Model 12-VK11)
Ch. TS-30, A (See Model 12VK15)
Ch. TS-52 (See Model 16K21)
Ch. TS-53 (See Model 12K21)
Ch. TS-60 (See Model 16F1)
Ch. TS-67 (See Model 19F1)
Ch. TS-74 (See Model 16K2)
Ch. TS-88 (See Model 14K1)
Ch. TS-94 (See Model 16F8B)
Ch. TS-98 (See Model 16K2BH)
Ch. TS-95 (See Model 17K1A)
Ch. TS-101 (See Model 19K21)
Ch. TS-114A (See Model 14T3X1)
Ch. TS-115 (See Model 14K1BH)
Ch. TS-118 (See Model 16K1)
Ch. TS-118A, B (See Model 17T3X1)
Ch. TS-119, A (See Model 19K2E)
Ch. TS-119B (See Model 20F2)
Ch. TS-119C, C1, D (See Model 20K3)
Ch. TS-172 (See Model 17K18E)
Ch. TS-174 (See Model 17F68C)
Ch. TS-214 (See Model 17T5A)
Ch. TS-216 (See Model 14T4)
Ch. TS-220 (See Model 17K9)
Ch. TS-221, A (See Model 17K5E)
Ch. TS-228 (See Model 17F1)
Ch. TS-236 (See Model 17K8)
Ch. TS-275 (See Model 14P2)
Ch. TS-292A, B, C (See Model 21C1)
Ch. TS-292AY, BY, CY (See Model 21C1Y)
Ch. TS-307 (See Model 20K6)

MOTOROLA—Cont.

Ch. TS-314A, B, TS-315A, B (See Model 17K10E)
Ch. TS-324, A, B (See Model 21T4A)
Ch. TS-324AY, BY (See Models 21T4A and TK-19M)
Ch. TS-325, A, TS-326, A (See Model 17F12)
Ch. TS-326AY (See Models 17F12 and VK-17M)
Ch. TS-351, A, B (See Model 21F1)
Ch. TS-395, -02 (See Model 17F13)
Ch. TS-400A (See Model 17T11E)
Ch. TS-401 (See Model 17K17)
Ch. TS-402 (See Model 17K17)
Ch. TS-402Y (See Model 17K17)
Ch. TS-408A (See Model 17F13C)
Ch. TS-408Y (See Models 17F13C and TK-19M)
Ch. TS-410A (See Model 17T13)
Ch. TS-410Y (See Model 17T13)
Ch. TS-501A (See Model 21T3)
Ch. TS-501Y (See Models 21T3 and TK-24M)
Ch. TS-502 (See Model 21C2)
Ch. TS-502Y (See Model Y21C2)
Ch. TS-602 (See Model 24K11)
Ch. TS-602Y (See Model Y24K11)
Ch. TS-502Y (See Model 21T8A)
Ch. TS-502Y (See Model Y21T8A)
Ch. TS-292A, AY, B, BY, C, CY (See Model 21K10, Y)
Ch. TS-402 (See Model 17T15A)
Ch. TS-402Y (See Model 17T15A)
Ch. VTS-410 (See Model 17T14)
Ch. VTS-410Y (See Model 17T14Y)
Ch. VTS-502 (See Model 21T11)
Ch. VTS-502Y (See Model Y21T11)
Ch. WTS-292A, AY, B, BY, C, CY (See Model 21K10, Y)
Ch. WTS-502 (See Model 21K12A)
Ch. WTS-502Y (See Model Y21K12A)
Ch. 1A 134-8
Ch. 1B 136-11
Ch. 2A 197-7
Ch. 2B 197-7
Ch. 8A 46-16
Ch. 10A 106-10
M30 (Ch. TV-16A1) Tel. Rec. 108-8
M31 (Ch. TV-16A2) Tel. Rec. 108-8
M31R (Ch. TV17A2) Tel. Rec. 116-10
M31R (Ch. TV17A3) Tel. Rec. (See Model M32 (Ch. TV17A3)—Set 116-10)
M31R, M32 (Ch. TV-16A3) Tel. Rec. 108-8
M32 (Ch. TV17A2) Tel. Rec. 116-10
M32 (Ch. TV17A3) Tel. Rec. 116-10
M32R (Ch. TV17A3) Tel. Rec. (See Model M32 (Ch. TV17A3)—Set 116-10)
M33 (Ch. TV17A4) Tel. Rec. 116-10
M34 (Ch. TV17A4) Tel. Rec. (For TV Ch. only see Model M33—Set 116-10)
M41, M42 (Ch. TV17A3A) Tel. Rec. (See Model 1750)
M44 (Ch. TV17A7) Tel. Rec. (See Model 2053)
M49 (Ch. TV17A7) Tel. Rec. (See Model 2053)
M-158 Tel. Rec. 97A-10
M-159A, B Tel. Rec. 97A-10
M-169 Tel. Rec. 96-6
31771 (Ch. 37C4) Tel. Rec. 236-9
31772 (Ch. 37A2) Tel. Rec. (See Model 2055—Set 207-5)
321 (Ch. 37A4) Tel. Rec. 236-9
321D1 (Ch. 37A4) Tel. Rec. 236-9
321T1, 321T2 (Ch. 17B2) Tel. Rec. (See Model 2055—Set 207-5)
321T3 (Ch. 37B4) Tel. Rec. 236-9
321T4 (Ch. 37A4) Tel. Rec. 236-9
321T5 (Ch. 37B4) Tel. Rec. 236-9
324T2 (Ch. 1788, Above Serial No. 374500) Tel. Rec. (See PCB 87—Set 230-1 and Model 2763A—Set 208-7)
327T2 (Ch. 1788, Above Serial No. 369500) or Ch. 1786, Above Serial No. 3619500) Tel. Rec. 207-5
2055-A (Ch. 1781, 1782) Tel. Rec. (See Ch. 1781—Set 163-8)
2055A, AU (Ch. 1782, Above Serial No. 369500 or Ch. 1786, Above Serial No. 3619500) Tel. Rec. 207-5
2055-B (Ch. 1781, 1782) Tel. Rec. (See Ch. 1782—Set 163-8)
2055C (Ch. 1782, Above Serial No. 369500 or Ch. 1786, Above Serial No. 3619500) Tel. Rec. 207-5
2056 (Ch. 17A7) Tel. Rec. (See PCB 33—Set 159-3 and Model M31—Set 116-10)
2056-A (Ch. 1781, 1782) Tel. Rec. (See Ch. 1781—Set 163-8)
2060 Tel. Rec. 164-6

NOTE: PCB denotes Production Change Bulletin

MUNTZ-PHILCO

MUNTZ-Cont.

2066 [Ch. 17B2, Above Serial No. 369500 or Ch. 17B6, Above Serial No. 3619500] Tel. Rec. 207-5
2158A [Ch. 17B2, Above Serial No. 369500 or Ch. 17B6, Above Serial No. 3619500] Tel. Rec. 207-5
2158-A [Ch. 17B5, 17B6] Tel. Rec. [See Ch. 17B5-Set 163-8]
2159A [Ch. 17B2, Above Serial No. 369500 or Ch. 17B6, Above Serial No. 3619500] Tel. Rec. 207-5
2159-A [Ch. 17B5, 17B6] Tel. Rec. [See Ch. 17B5-Set 163-8]
2162 [Ch. 17B2 Above Serial No. 369500 or Ch. 17B6, Above Serial No. 3619500] Tel. Rec. 207-5
2162-A [Ch. 17B5, 17B6] Tel. Rec. [See Ch. 17B5-Set 163-8]
2457-A [Ch. 17B3, 17B4] Tel. Rec. [See Ch. 17B3-Set 163-8]
2461-A [Ch. 17B3, 17B4] Tel. Rec. [See Ch. 17B3-Set 163-8]
2763A, 2764A, 2765A [Ch. 17B8, Above Serial No. 374500] Tel. Rec. 207-5
2763-1 [See Model 374500-Set 230-1]
Ch. 17B1, 17B2 Tel. Rec. 163-8
Ch. 17B2 (Above Serial No. 369500) [See Model 2055]
Ch. 17B3, 17B4, 17B5, 17B6 Tel. Rec. 163-8
Ch. 17B6 (Above Serial No. 3619500) [See Model 2055]
Ch. 17B8 (Above Serial No. 374500) [See Model 2763A]
Ch. 37A2 [See Model 31772]
Ch. 37A4 [See Model 321C1]
Ch. 37B4 [See Model 321T3]
Ch. 37C4 [See Model 317T1]

MURPHY

113 2-2
122 [See Model 112-Set 2-15]

MUSTRON

PT-10 15-20
PX 16-28
SRC-3 13-21
101 "Piccola" 13-21
103 "Piccola" 15-21
105 21-26
202 21-27

MUTUAL BUYING SYNDICATE

(See Drexel or General)

NASH

AC-152 (NH2AC) 184-9
NH3C 216-6
6MNB82 9-25

NATIONAL CO.

HFS 62-14
HRO-7R, HRO-7T 50-12
HRO-50 112-7
HRO-50R1, HRO-50T1 169-11
HRO-60 202-4
NC-TV7, NC-TV7M, NC-TV7W Tel. Rec. 67-14
NC-TV-10C, T, W Tel. Rec. [Also see PCB 1-Set 103-19] 94-5
NC-TV-12C, W Tel. Rec. [Also see PCB 1-Set 103-19] 94-5
NC-TV-1001 Tel. Rec. [Also see PCB 1-Set 103-19] 94-5
NC-TV-1025 Tel. Rec. [Also see PCB 1-Set 103-19] 94-5
NC-TV-1201, NC-TV-1202 Tel. Rec. [Also see PCB 1-Set 103-19] 94-5
NC-TV-1225, NC-TV-1226 Tel. Rec. [Also see PCB 1-Set 103-19] 94-5
NC-2-40DR, NC-2-40DT 41-16
NC-33 47-14
NC-46 9-26
NC-57 48-14
NC-88 233-7
NC-108R, NC-108T 47-15
NC-125 139-10
NC-173R, NC-173T 40-13
NC-183R, NC-183T 49-15
SW-54 141-9
TV-1201 Tel. Rec. 119-10
TV-1226 Tel. Rec. 119-10
TV-1601 Tel. Rec. 119-10
TV-1625 Tel. Rec. 119-10
TV-1701, TV-1702 Tel. Rec. 145-7
TV-1725, TV-1727 Tel. Rec. 145-7
TV-1729, TV-1730, TV-1731, TV-1732 Tel. Rec. 145-7
TV-2029, TV-2030 Tel. Rec. 145-7

NATIONAL UNION

G-613 "Commuter" 19-23
G-619 11-35
571, 571A, 571B 17-22

NEWCOMB

A-104R 196-8
H-10 14-20
H-14 15-22
KX-30 15-23

NOBLITT SPARKS

(See Arvin)

NORELCO

PT200, PT300 Tel. Rec. 155-13
588A Tel. Rec. 164-7
1200A Tel. Rec. [See Model 588A-Set 164-7]

OK

(See Record Changer Listing)

OLDSMOBILE

982375 20-25
982399 59-14
982420 57-12
982421 87-7
982454 60-16
982543 157-7
982544, 982573 96-7
982579 157-7
982697, 982698 [See Model 982544-Set 96-7]

OLDSMOBILE-Cont.

2066 [Ch. 17B2, Above Serial No. 369500 or Ch. 17B6, Above Serial No. 3619500] Tel. Rec. 207-5
2158A [Ch. 17B2, Above Serial No. 369500 or Ch. 17B6, Above Serial No. 3619500] Tel. Rec. 207-5
2158-A [Ch. 17B5, 17B6] Tel. Rec. [See Ch. 17B5-Set 163-8]
2159A [Ch. 17B2, Above Serial No. 369500 or Ch. 17B6, Above Serial No. 3619500] Tel. Rec. 207-5
2159-A [Ch. 17B5, 17B6] Tel. Rec. [See Ch. 17B5-Set 163-8]
2162 [Ch. 17B2 Above Serial No. 369500 or Ch. 17B6, Above Serial No. 3619500] Tel. Rec. 207-5
2162-A [Ch. 17B5, 17B6] Tel. Rec. [See Ch. 17B5-Set 163-8]
2457-A [Ch. 17B3, 17B4] Tel. Rec. [See Ch. 17B3-Set 163-8]
2461-A [Ch. 17B3, 17B4] Tel. Rec. [See Ch. 17B3-Set 163-8]
2763A, 2764A, 2765A [Ch. 17B8, Above Serial No. 374500] Tel. Rec. 207-5
2763-1 [See Model 374500-Set 230-1]
Ch. 17B1, 17B2 Tel. Rec. 163-8
Ch. 17B2 (Above Serial No. 369500) [See Model 2055]
Ch. 17B3, 17B4, 17B5, 17B6 Tel. Rec. 163-8
Ch. 17B6 (Above Serial No. 3619500) [See Model 2055]
Ch. 17B8 (Above Serial No. 374500) [See Model 2763A]
Ch. 37A2 [See Model 31772]
Ch. 37A4 [See Model 321C1]
Ch. 37B4 [See Model 321T3]
Ch. 37C4 [See Model 317T1]

OLYMPIC

DX-214, DX-215, DX-216 Tel. Rec. 106-11
DX-619, DX-620, DX-621, DX-622 Tel. Rec. 106-11
DX-911, DX-932 Tel. Rec. 106-11
DX-950 Tel. Rec. 106-11
RTU-3M (Dupliator) 62-15
TV-104, TV-105 Tel. Rec. 67-15
TV-106, TV-107, TV-108 Tel. Rec. [See Model TV-104-Set 67-15]
TV-922 Tel. Rec. 58-14
TV-922L Tel. Rec. 67-15
TV-928 Tel. Rec. [See Model TV-922-Set 58-14]
TV-944, TV-945 Tel. Rec. 67-15
TV-946 Tel. Rec. [See Model TV-944-Set 67-15]
TV-947 Tel. Rec. 85-10
TV-948 Tel. Rec. [See Model TV-104-Set 67-15]
TV-949, TV-950 Tel. Rec. 85-10
XL-210, XL-211 Tel. Rec. 109-8
XL-612, XL-613 Tel. Rec. 109-8
6-501, 6-502, 6-503, 6-504 4-10
6-501-U [See Model 6-501-U-Set 3-20]
6-501-W, 6-502-U 3-20
6-504, 6-504L 3-25
6-601W, 6-601V, 6-602 8-24
6-604 Series 22-7
6-604V-110, 6-604V-220, 6-604W-110, 6-604W-150, 6-604-220 [See Model 6-604 Series-Set 22-21]
6-606 4-36
6-606-A 11-17
6-606-U 11-18
6-717 4-7
6-617U [See Model 6-617-Set 4-7]
7-421V, 7-421W, 7-421X 57-13
7-435V, 7-435W 34-13
7-526 30-21
7-532W, 7-532V 37-13
7-537 37-13
7-622, 7-638 34-14
7-724 29-19
7-728 [See Model 7-724-Set 29-19]
7-925, 7-934, 7-936, 7-939 31-22
8-45 48-15
8-533V, 8-533W 57-14
8-618 35-16
8-925, 8-934, 8-936 45-19
9-435V, 9-435W 152-11
17C Tel. Rec. [See Model 752-Set 17C-8]
17C24 Tel. Rec. 182-7
17C44 [Ch. TK17] Tel. Rec. 196-9
17C57 [Ch. TM-17] Tel. Rec. 216-7
17D Tel. Rec. [See Model 752-Set 17D-7]
17K13, 17K32 Tel. Rec. 182-6
17K41, 17K42 [Ch. TK17] Tel. Rec. 196-9
17K50 [Ch. TM-17] Tel. Rec. 216-7
17T20 Tel. Rec. 182-6
17T33 Tel. Rec. 182-6
17T40 [Ch. TK17] Tel. Rec. 196-9
17T48 [Ch. TK17] Tel. Rec. 196-9
17T56 [Ch. TM-17] Tel. Rec. 216-7
20C45 [Ch. TL20] Tel. Rec. 196-9
20C52, 20C53 [Ch. TL20] Tel. Rec. 196-9
20D49 [Ch. TL20] Tel. Rec. 196-9
20K43 [Ch. TL20] Tel. Rec. 196-9
20K51 [Ch. TL20] Tel. Rec. 196-9
20T46, 20T47 [Ch. TL20] Tel. Rec. 196-9
21C28 Tel. Rec. 214-7
21C65, 21C68 [Ch. TN-21] Tel. Rec. 214-7
21C72, 21C73 [Ch. TN-21] Tel. Rec. 214-7
21D29 Tel. Rec. 182-7
21D60, 21D64 [Ch. TN-21] Tel. Rec. 214-7
21K26 Tel. Rec. 182-7
21K61, 21K62, 21K63B [Ch. TN-21] Tel. Rec. 214-7
21T27 Tel. Rec. 182-7
21T58 [Ch. TN-21] Tel. Rec. 214-7
21T69, 21T70 [Ch. TN-21] Tel. Rec. 214-7
21T74 [Ch. TN-21] Tel. Rec. 214-7
51-421W 151-9
489 154-9
51-435-W [See Model 9-435W-Set 152-11]
752, 752U, 753, 753U Tel. Rec. 126-8
754 Tel. Rec. [See Model 752-Set 126-8]
755, 755U Tel. Rec. 126-8
757 Tel. Rec. [See Model 752-Set 126-8]
758 Tel. Rec. [See Model 752-Set 126-8]
762 Tel. Rec. 139-11
764, 764U Tel. Rec. 126-8
765, 766 Tel. Rec. [See Model 752-Set 126-8]
767 Tel. Rec. 126-8
768, 769, 773 Tel. Rec. [See Model 752-Set 126-8]
783 Tel. Rec. 139-11
785 Tel. Rec. [See Model 762-Set 139-11]
791, 792 Tel. Rec. [See Model 752-Set 126-8]
967, 968, 970 Tel. Rec. 139-11
Ch. TK17 [See Model 17T40]
Ch. TL20 [See Model 20C45]
Ch. TM-17 [See Model 17C57]
Ch. TN-21 [See Model 21C65]

OPERADIO

1A30 34-15
1A35 33-15
1A45 48-16
1A65 52-14
982699, 982700 150-10
982990 225-13
983004 235-8

OPERADIO-Cont.

1A70-A 47-16
1A140 46-17
4A25-E 101-8
4A30-A 101-9
4A35 100-9
4A50-A, 4A51-A 102-9
4A55 100-9
4M25C 99-11
11A55 113-6
530, 531, 1335 "Soundcast" 37-14

ORTHOSONIC

(See Electronic Labs.)

PACIFIC MERCURY

(See Mercury)

PACKARD

PA-382042 20-26
621-393607 57-15
416387 160-7
416394 145-8
439279 [See PCB 104-Set 250-1 and Model 416387-Set 160-7]
439310 [See PCB 104-Set 250-1 and Model 416387-Set 160-7]
439338, 439339 160-7
439661 [See PCB 104-Set 250-1 and Model 416387-Set 160-7]
439663 [See PCB 101-Set 247-1 and Model 439338-Set 229-8]
439665 [See PCB 104-Set 250-1 and Model 416387-Set 160-7]
439666 [See PCB 101-Set 247-1 and Model 439338-Set 229-8]

PACKARD-BELL

C1362 12-21
C1461 12-22
SDA 16-29
SDB 44-15
5FP 1-29
100 53-16
203-1 23-28
471 30-22
531 231-11
532 232-4
551-D [See Model 551-Set 2-7]
561 22-35
563 [See Model 561-Set 2-35]
568 [See Model 551-Set 2-7]
568 19-24
571 [See Model 572-Set 22-22]
572 22-22
581 [See Model 508-Set 44-15]
606-U 182-8
651 8-25
661 4-42
662 13-22
673A, 673B 46-18
682 54-16
683 47-14
861 17-23
872 31-23
880, 880A 46-16
881-A, 881-B 47-17
884, 892 74-7
1052, 1052A 8-26
1054B 13-23
1063 18-25
1181, 1181A 75-12
1273 46-19
1472 48-17
2001TV, 2002TV Tel. Rec. 204-1
2041, 2042, 2043, 2044 [Ch. 2040] Tel. Rec. 233-8
2101, 2102 Tel. Rec. 123-10
2105, 2105A Tel. Rec. 123-10
2115, 2116 [Ch. 2115-2] Tel. Rec. 195-9
2117 [Ch. 2117] Tel. Rec. 195-9
2118 Tel. Rec. 204-7
2141, 2142, 2143, 2144 [Ch. 2040] Tel. Rec. 233-8
2202, 2204 Tel. Rec. 123-10
2291TV, 2292TV, 2293TV, 2294TV, 2295TV, 2296TV Tel. Rec. 82-10
2297-TV De Luxe, 2297-TV Standard, 2297 82-10
2298-TV Tel. Rec. 82-10
2301-TV Tel. Rec. 126-9
2302 Tel. Rec. [See Model 2301-Set 26-9]
2311 Tel. Rec. 161-6
2421, 2422, 2423 Tel. Rec. 187-9
2601-TV Tel. Rec. 122-6
2602 Tel. Rec. 123-10
2621, 2622 [Ch. 2621-2] Tel. Rec. 186-10
2692-TV Tel. Rec. 122-7
2721, 2722 [Ch. 2720] Tel. Rec. 207-6
2723, 2724 [Ch. 2710] Tel. Rec. 207-6
2742, 2743 [Ch. 2740] Tel. Rec. 238-10
2801-TV, 2801A-TV Tel. Rec. 126-9
2803TV Tel. Rec. 129-8
2811A Tel. Rec. 161-6
2841 [Ch. 2840] Tel. Rec. 242-7
2842, 2843, 2844 [Ch. 2740] Tel. Rec. 238-10
2846, 2847 [Ch. 2840] Tel. Rec. [See Model 2841-Set 242-7]
2921, 2922 Tel. Rec. 213-4
2941 [Ch. 2940-1] Tel. Rec. 238-10
2942 [Ch. 2840] Tel. Rec. 242-7
2946, 2947 [Ch. 2840] Tel. Rec. [See Model 2841-Set 242-7]
2991TV Tel. Rec. 94-6
3041 [Ch. 2940-1] Tel. Rec. 238-10
3042 [Ch. 3040-1] Tel. Rec. 242-7
3142 [Ch. 3040-1] Tel. Rec. 242-7
Ch. 2040 [See Model 2041]
Ch. 2115-2 [See Model 2115]
Ch. 2621-2 [See Model 2621]
Ch. 2710 [See Model 2723]
Ch. 2720 [See Model 2721]
Ch. 2740 [See Model 2742]
Ch. 2840 [See Model 2841]
Ch. 2940-1 [See Model 2941]
Ch. 3040-1 [See Model 3042]

PARKVIEW

17X Tel. Rec. 185-9

PATHE

17-N25, 17-RPC, 17-RPT [Ch. TAP] Tel. Rec. [Similar to Chassis] 127-12

PENTRON

(Also see Recorder Listing)

AM-Y 183-11
F-100 184-10
MM4 178-8

PHILCO

(Also see Record Changer Listing)

A-T1814 [Code 123] [Ch. 81, H-1, H-1A] Tel. Rec. [See PCB 83-Set 203-1, PCB 82-Set 223-1 and Model 53-T1853-Set 185-10]
A-T1816, L [Code 123] [Ch. 81, H-1, H-1A] Tel. Rec. [See PCB 83-Set 203-1, PCB 82-Set 223-1 and Model 53-T1853-Set 185-10]
A-T1816, L [Code 129] [Ch. 81A, D-81] Tel. Rec. 227-10
A-T1817, HM [Code 123] [Ch. 81, H-1, H-1A] Tel. Rec. [See PCB 83-Set 203-1, PCB 82-Set 223-1 and Model 53-T1824-Set 201-7]
A-T1818 [Code 128] [Ch. 91A, J-2] Tel. Rec. [See PCB 66-Set 203-1, PCB 82-Set 223-1 and Model 53-T1853-Set 185-10]
A-T1856, HM, L, W [Code 123] [Ch. 81, H-1, H-1A] Tel. Rec. [See PCB 83-Set 203-1, PCB 82-Set 223-1 and Model 53-T1824-Set 201-7, for UHF Tuner see Model UT218-Set 223-9]
A-T1856W [Code 129] [Ch. 81A, D-81] Tel. Rec. 227-10
A-T1858 [Code 128] [Ch. 91A, J-2] Tel. Rec. [See PCB 66-Set 203-1, PCB 82-Set 223-1 and Model 53-T1853-Set 185-10]
A-T2230, L [Code 123] [Ch. 81, H-1, H-1A] Tel. Rec. [See PCB 83-Set 203-1, PCB 82-Set 223-1 and Model 53-T1824-Set 201-7]
A-T2230, L [Code 129] [Ch. 81A, D-81] Tel. Rec. 227-10
A-T2232 [Code 123] [Ch. 81, H-1, H-1A] Tel. Rec. [See PCB 83-Set 203-1, PCB 82-Set 223-1 and Model 53-T1824-Set 201-7]
A-T2233 [Code 128] [Ch. 91A, J-2] Tel. Rec. [See PCB 66-Set 203-1, PCB 82-Set 223-1 and Model 53-T1853-Set 185-10]
A-T2266, L [Code 123] [Ch. 81, H-1, H-1A] Tel. Rec. [See PCB 83-Set 203-1, PCB 82-Set 223-1 and Model 53-T1824-Set 201-7]
A-T2266, L [Code 128] [Ch. 91A, J-2] Tel. Rec. [See PCB 66-Set 203-1, PCB 82-Set 223-1 and Model 53-T1853-Set 185-10]
A-T2271HM [Code 128] [Ch. 91A, J-2] Tel. Rec. [See PCB 66-Set 203-1, PCB 82-Set 223-1 and Model 53-T1853-Set 185-10]
A-T2272, L [Code 123] [Ch. 81, H-1, H-1A] Tel. Rec. [See PCB 83-Set 203-1, PCB 82-Set 223-1 and Model 53-T1824-Set 201-7]
A-T2272, L [Code 129] [Ch. 81A, D-81] Tel. Rec. 227-10
A-T2274, W [Code 123] [Ch. 81, H-1, H-1A] Tel. Rec. [See PCB 83-Set 203-1, PCB 82-Set 223-1 and Model 53-T1824-Set 201-7, for UHF Tuner see Model UT218-Set 223-9]
A-T2274S [Code 128] [Ch. 91A, J-2] Tel. Rec. [See PCB 66-Set 203-1, PCB 82-Set 223-1 and Model 53-T1853-Set 185-10]
A-T2275S [Code 129] [Ch. 81A, D-81] Tel. Rec. 227-10
A-T2277, L [Code 123] [Ch. 81, H-1, H-1A] Tel. Rec. [See PCB 83-Set 203-1, PCB 82-Set 223-1 and Model 53-T1824-Set 201-7]
A-T2277S [Code 128] [Ch. 91A, J-2] Tel. Rec. [See PCB 66-Set 203-1, PCB 82-Set 223-1 and Model 53-T1853-Set 185-10]
A-T2279 [Code 123] [Ch. 81, H-1, H-1A] Tel. Rec. [See PCB 83-Set 203-1, PCB 82-Set 223-1 and Model 53-T1824-Set 201-7]
A-T2280 [Code 128] [Ch. 91A, J-2] Tel. Rec. [See PCB 66-Set 203-1, PCB 82-Set 223-1 and Model 53-T1853-Set 185-10]
A-T2282, L [Code 123] [Ch. 81, H-1, H-1A] Tel. Rec. [See PCB 83-Set 203-1, PCB 82-Set 223-1 and Model 53-T1824-Set 201-7, for UHF Tuner see Model UT218-Set 223-9]
A-T2282, L [Code 129] [Ch. 81A, D-81] Tel. Rec. 227-10
A-T2288, HM [Code 123] [Ch. 81, H-1, H-1A] Tel. Rec. [See PCB 83-Set 203-1, PCB 82-Set 223-1 and Model 53-T1824-Set 201-7]
A-T2288HM, S [Code 128] [Ch. 91A, J-2] Tel. Rec. [See PCB 66-Set 203-1, PCB 82-Set 223-1 and Model 53-T1853-Set 185-10]
A-T2292, L [Code 123] [Ch. 81, H-1, H-1A] Tel. Rec. [See PCB 83-Set 203-1, PCB 82-Set 223-1 and Model 53-T1824-Set 201-7]
A-T2292, L [Code 128] [Ch. 91A, J-2] Tel. Rec. [See PCB 66-Set 203-1, PCB 82-Set 223-1 and Model 53-T1853-Set 185-10]
A-T2292L [Code 128] [Ch. 94A, J-5 and Radio Ch. RT-10] Tel. Rec. [For TV Ch. Only See PCB 85-Set 226-1 and Model 53-T285-Set 213-5]
A-T2299 [Code 121] [See Model B570-Set 228-13]
B574 [Code 121] 229-9
B649 [See Model B650-Set 226-5]
B650 [See Model 52-640-Set 153-12]
B-652 234-10
B656 [See Model 53-656-Set 187-10]
B710 [Code 121] [See Model B710-Set 223-8]
B712 [Code 121] [See Model 53-701-Set 193-6]
B714 [Code 121, 123] 229-10
B714X [Code 121] 229-10
B804 [See Model 53-804-Set 210-4]
B-856 218-8
B1350 [See Model 53-1350-Set 203-7]
B-1352 235-9
B1750 [See Model 53-1750-Set 203-7]
B1752 240-6
B1753 240-6
B1754 [See Model 53-1754-Set 214-8]
B1756 241-10
C-4608 [Code 121] [See Mopar Model 802-Set 18-24]
C-4608 [Code 122] [See Mopar Model 802 Revised-Set 42-19]
C-4908 [See Mopar Model 805-Set 71-11]
C-5009 [See Mopar Model 809-Set 71-11]
C-5010 [See Mopar Model 805-Set 71-11]
C-5109 [See Mopar Model 815-Set 139-8]
C-5110 [See Mopar Model 816-Set 139-8]

PHILCO-Cont.

A-UT1817 [Code 123] [Ch. 81, H-1, H-1A] Tel. Rec. [For TV Ch. see PCB 83-Set 203-1, and Model 53-T1824-Set 201-7, for UHF Tuner see Model UT218-Set 223-9]
A-UT1818 [Code 128] [Ch. 91A, J-2] Tel. Rec. [See PCB 66-Set 203-1, PCB 82-Set 223-1 and Model 53-T1853-Set 185-10]
A-UT1856, HM, L, W [Code 123] [Ch. 81, H-1, H-1A] Tel. Rec. [For TV Ch. see PCB 83-Set 203-1, PCB 82-Set 223-1 and Model 53-T1824-Set 201-7, for UHF Tuner see Model UT218-Set 223-9]
A-UT2232 [Code 123] [Ch. 81, H-1, H-1A] Tel. Rec. [For TV Ch. see PCB 83-Set 203-1, PCB 82-Set 223-1 and Model 53-T1824-Set 201-7, for UHF Tuner see Model UT218-Set 223-9]
A-UT2233 [Code 128] [Ch. 91A, J-2] Tel. Rec. [See PCB 66-Set 203-1, PCB 82-Set 223-1 and Model 53-T1853-Set 185-10]
A-UT2266, L [Code 128] [Ch. 91A, J-2] Tel. Rec. [See PCB 66-Set 203-1, PCB 82-Set 223-1 and Model 53-T1853-Set 185-10]
A-UT2272 [Code 123] [Ch. 81, H-1, H-1A] Tel. Rec. [For TV Ch. see PCB 83-Set 203-1, PCB 82-Set 223-1 and Model 53-T1824-Set 201-7, for UHF Tuner see Model UT218-Set 223-9]
A-UT2272 [Code 129] [Ch. 81A, D-81] Tel. Rec.

RCA VICTOR—REGAL

RCA VICTOR—Cont.

Ch. RC-610 (See Model 610V1)
 Ch. RC610A, RC610B (See Model 730TV1)
 Ch. RC610C (See Model 610V1)
 Ch. RC613A (See Model 710V2)
 Ch. RC-613 (See Model 7V11)
 Ch. RC-616 (See Model 8V111)
 Ch. RC-616A, RC-616H (See Model 8V91)
 Ch. RC616B, C, J, K (See Model 8V321)
 Ch. RC-616N (See Model 9V7W333)
 Ch. RC617A, RC-618 (See Model S1000)
 Ch. RC-618, RC-618A (See Model 8V90)
 Ch. RC-618, B, C (See Model 9V101)
 Ch. RC-622 (See Model A106)
 Ch. RC-1004E (See Model 55F)
 Ch. RC-1011 (See Model 56K)
 Ch. RC-1017 (See Model 55AU)
 Ch. RC-1017A (See Model 65AU)
 Ch. RC-1023B (See Model 56X10)
 Ch. RC-1034 (See Model 65X1)
 Ch. RC-1037, RC-1037A (See Model 64F1)
 Ch. RC-1037B (See Model 8F43)
 Ch. RC-1038, RC-1038A (See Model 66X1)
 Ch. RC-1040, RC-1040A (See Model 66X8)
 Ch. RC-1040C (See Model 88X6)
 Ch. RC-1045 (See Model 65B9)
 Ch. RC-1046, A, B (See Model 66X11)
 Ch. RC-1047 (See Model 54B5)
 Ch. RC-1050, RC-1050B (See Model 75X11)
 Ch. RC-1057A (See Model 77U)
 Ch. RC-1057B (See Model 9V7)
 Ch. RC-1059 (See Model 88X5)
 Ch. RC-1059B, RC-1059C (See Model 98X5)
 Ch. RC-1060 (See Model 8R71)
 Ch. RC-1060A (See Model 8R72)
 Ch. RC-1061 (See Model 8K681)
 Ch. RC-1064 (See Model 8K53)
 Ch. RC-1064 (See Model 65X1)
 Ch. RC-1065, RC-1065A (See Model 8K541)
 Ch. RC-1066 (See Model 8K521)
 Ch. RC-1066A (See Model 8K522)
 Ch. RC-1068 (See Model 9K56)
 Ch. RC-1069A, B (See Model 8841)
 Ch. RC-1070 (See Model 8X71)
 Ch. RC-1070A (See Model X711)
 Ch. RC-1077 (See Model 9Y51)
 Ch. RC-1077A, B (See Model 9Y510)
 Ch. RC-1079, A (See Model 9K571)
 Ch. RC-1079B, RC-1079C (See Model 9X561)
 Ch. RC-1079K, L (See Model 1X591)
 Ch. RC-1080C (See Model 2X61)
 Ch. RC-1080D (See Model 2X62)
 Ch. RC-1082 (See Model 8X6)
 Ch. RC-1085, RC-1085A (See Model 9X651)
 Ch. RC-1085B (See Model 2X621)
 Ch. RC-1087 (See Model 8X55)
 Ch. RC-1088, RC-1088A (See Model 8X55)
 Ch. RC-1089B, C (See Model X551)
 Ch. RC-1090 (See Model 4T141)
 Ch. RC-1092 (See Model 9T89)
 Ch. RC-1094 (See Model A-8)
 Ch. RC-1096 (See Model A-108)
 Ch. RC-1096A (See Model 45-W-10)
 Ch. RC-1098 (See Model 8411)
 Ch. RC-1098A (See Model B-411)
 Ch. RC-1102 (See Model 1881)
 Ch. RC-1104, 1, A, B, B-1, C, D, E (See Model 1X51)
 Ch. RC-1110 (See Model PK600)
 Ch. RC-1111 (See Model 2510)
 Ch. RC-1111A (See Model 21D346)
 Ch. RC-1111B (See Model 21D346)
 Ch. RC-1111C (See Model 21D393)
 Ch. RC-1114 (See Model 28400)
 Ch. RC-1115 (See Model 28X63)
 Ch. RC-1117A (See Model 2U57)
 Ch. RC-1117B (See Model 21T242)
 Ch. RC-1117C (See Model 28F57)
 Ch. RC-1117D (See Model 2-S-7)
 Ch. RC-1118, A, B, C (See Model 2C511)
 Ch. RC-1119 (See Model 2R51)
 Ch. RC-1120, A (See Model 2C521)
 Ch. RC-1121 (See Model 2R51)
 Ch. RC-1121A (See Model 2X9F931)
 Ch. RC-1125 (See Model 38X671)
 Ch. RC-1126 (See Model 38X51)
 Ch. RC-1128 (See Model 3X521)
 Ch. RC-1129 (See Model 3R9F1)
 Ch. RC-117 (See Model 64BV)
 Ch. RK-117A (See Model 8TV41)
 Ch. RK-121 (See Model 612V1)
 Ch. RK-121A (See Model 64BPTK)
 Ch. RK-121C (See Model RV151)
 Ch. RK-135, RK-135A (See Model 8T29)
 Ch. RK-135A-1 (See Model 8TK320)
 Ch. RK-135C (See Model 9TW309)
 Ch. RK-135D (See Model TA1A9)
 Ch. RS-123 (See Model 612V1)
 Ch. RS-123A (See Model 9V61A)
 Ch. RS-123B (See Model 64BV)
 Ch. RS-123C (See Model 8PC541)
 Ch. RS-123D (See Model RV151)
 Ch. RS-126 (See Model 66E)
 Ch. RS-127 (See Model 63E)
 Ch. RS-132 (See Model 9E73)
 Ch. RS-132F, H (See Model 45EY1)
 Ch. RS-132H (See Model 45EY-15)
 Ch. RS-138, A, H (See Model 45EY-2)
 Ch. RS-138L, M (See Model 45EY-26)
 Ch. RS-140 (See Model 45EY-4)
 Ch. RS-141 (See Model 2510)
 Ch. RS141A (See Model 21D346, U or Model 21T197DE)
 Ch. RS-141C (See Model 21T244)
 Ch. RS141D (See Model 21T393)
 Ch. RS-142 (See Model 2E53)
 Ch. RS-145, X (See Model 3-HS-6)
 Ch. RS-146 (See Model 3-HES-5)

RCA VICTOR—Cont.

Ainsworth (See Model 17T261DE)
 Brett (See Model 17T20E)
 Ashton (See Model 17T211)
 Bancraft (See Model 21T174DE)
 Barnes (See Model 21S359, GU)
 Barrett (See Model 24T420, U)
 Barton (See Models 21S353, G, GU)
 Belgrave (See Model 21T229)
 Bentley (See Model 4T101)
 Benton (See Model 21T175DE)
 Blake (See Models 21S354, G, GU, U)
 Brandon (See Model 21T228)
 Britz (See Model 17T250DE)
 Bristol (See Model 17T153)
 Brookfield (See Model 21T217)
 Cabot (See Model 21D305, U)
 Caldwell (See Model 17T162)
 Calhoun (See Model 17T173, 17T-173K)
 Camers (See Models 21S355, G, GU, U)
 Clarendon (See Model 21T179, DE)
 Clermont (See Model 21D330, U)
 Colby (See Model 17T150)
 Copeland (See Model 27D383, U)
 Coville (See Model 17T172, 17T172K)
 Crafton (See Model 17T163)
 Crandell (See Model 21T207, G)
 Cumberland (See Model 2T60)
 Deauville (See Model 21T315, U)
 Dobson (See Model 21T322, U)
 Donley (See Model 21T177)
 Fairfax (See Model 6T84)
 Fairfield (See Model 6T71, 6T72, 7T122, 7T122B)
 Farmington (See Model 21T166DE)
 Farrell (See Models 21S369, G, GU, U)
 Fitz (See Models 21S367, G, GU, U)
 Glenside (See Model 17T302)
 Glenside (See Model 17T151)
 Hadley (See Model 17T201)
 Hampton (See Model 17T160)
 Hanley (See Model 17T310)
 Hartford (See Model 6T87)
 Hayward (See Model 7T111B)
 Highland (See Model 6T65, 7T112, 7T112B)
 Hillside (See Model 9T77, 9T126)
 Hilton (See Model 21T316, U)
 Jeffrey (See Model 21T313, U)
 Kenbridge (See Model 21D32B, U)
 Kendall (See Model 17T174, 17T-174K)
 Kent (See Model 6T54, 7T104, 7T104)
 Kentwood (See Model 17T202)
 Kingsbury (See Model 6T64)
 Kirby (See Model 21T303, U)
 Lambert (See Model 21T208)
 Lexington (See Model 21T323, U)
 Lindale (See Model 21T227)
 Longchamps (See Model 27D384, U)
 Master 21 (See Models 21S348, G, GU, U)
 Meredith (See Model 21T165)
 Meritt (See Model 21D317, U)
 Madero (See Model 6T75, 7T124)
 Modernette (See Models 21S357, G, GU)
 Newport (See Models 6T53, 7T103)
 Northampton (See Model 9T79)
 Penley (See Model 21T244)
 Prentiss (See Model 21T314, U)
 Preston (See Model 17T155)
 Provincial (See Model 6T76, 7T-125B, 9T128)
 Regency (See Model 6T74, 7T123, 7T123B)
 Rockingham (See Models 21T178, 21T178DE)
 Rutherford (See Model 21D346)
 Rutland (See Model 6T86, 7T143)
 Sedgewick (See Model 9T89, 9T147)
 Selfridge (See Models 21T159, 21T59DE)
 Sewell (See Model 24T435, U)
 Shelby (See Model 2T51)
 Somerville (See Model 2T81, 4T141)
 Southbridge (See Model 21D329, U)
 Stanton (See Model 21D326, U)
 Stockton (See Model 21T324, U)
 Suffolk (See Model 21T176)
 Sunderland (See Model 21T197DE)
 Swathmore (See Model 27D382, U)
 Talbot (See Models 16T152, 21S362C, GU, M, MU)
 Wayne (See Model 17T301)
 Westland (See Model 21T242)
 Whitfield (See Model 17T154)
 Winston (See Model 17T132)
 York (See Model 9T57, 9T105)
 Yorktown (See Model 21D327, U)

RCA VICTOR—Cont.

DB-22A 50-14
 HF10-20 49-17
 VHF-2.11 79-14
 VHF-152A 51-18
 45 13-25
 84 14-13
 200 Tel. UHF Conv. 219-8

RADIO CRAFTSMEN

(Also see Craftsmen)
 C400 186-11
 RC-1 Tuner, RC-2 (Audio Amp.) 149-9
 "Kitchenaire" 39-14
 RC-8 66-13
 RC-10 110-12
 RC100 Tel. Rec. 96-9
 RC-100A Tel. Rec. (Also see PCB 39) 117-11
 RC101 Tel. Rec. 142-10
 RC200 Tel. Rec. (Also see PCB 40—Set 172-1) 150-9
 RC201 Tel. Rec. 176-3
 10 176-9
 202 Tel. Rec. 184-13
 500 164-8
 800 204-8

RADIO DEVELOPMENT & RESEARCH CO.

(See Magic-Tone)
 PR-2 50-15

RADIOLETTE

Y62W, Y728 26-22

RADIO MFG. ENGINEERS

(See RME)
 R-109-P Tel. UHF Conv. 222-12

RADIO WIRE TELEVISION

(See Lafayette)
 RANGER
 118 28-27

RANGERS

118 28-27

RAULAND

BAU21 211-10
 BA21 87-10
 W-819-A 43-16
 1801A 251-15
 1805A 251-15
 1810 179-10
 1814 99-13
 1820 100-10
 1821, 1822 59-17
 1825 148-11
 1824 (1801A, 1805) 251-15
 1835 60-17
 1841 58-19
 1904 140-10
 1916 229-12
 1917 7-18
 1940 208-9
 1961 212-4
 1960 (Sub-station) 39-20
 2101-A (Master Station) 39-20
 2103 (Master Station) 36-21
 2106-F 236-11
 2112-F 236-11
 2205, 2206H, 2212, 2212H, 2218, 2218H, 2224, 2224H 80-13
 2306, 2312, 2324 87-10
 2400 Series 33-12
 3406, H 210-6
 3412, H 210-6
 3424, H 210-6

RAY ENERGY

AD 7-24
 AD4 7-25
 SRB-1X 13-26

RAYTHEON (Also see Belmont)

A-7DX22P Tel. Rec. (See Model 7DX21—Set 81-13)
 A-10DX24, B-10DX22 Tel. Rec. (Also see PCB 1—Set 103-19) 75-14
 CR-41, A, CR-42, A, CR-43, A (Ch. 4D16-A) 212-5
 C1102 (Ch. 12AX22) Tel. Rec. (Also see PCB 3—Set 105-1) 94-8
 C1104 (Ch. 12AX22) Tel. Rec. (Also see PCB 3—Set 105-1) 94-8
 C-1104B (Ch. 12AX26, 12AX27) Tel. Rec. 141-11
 C-1401 (Ch. 14AX21) Tel. Rec. 123-6
 C-1602, A, B, C (Ch. 17AX23, 25, 26) Tel. Rec. 99-14
 C-1602, Series 2 (Ch. 17AX29) Tel. Rec. (See PCB 16—Set 126-1 and Model C-1602—Set 99-14)
 C-1614 (Ch. 16AY21) Tel. Rec. (See PCB 19—Set 132-1 and Model C-1615A—Set 124-8)
 C-1614B (Ch. 16AY28) Tel. Rec. (See PCB 19—Set 132-1 and Model C-1615B—Set 124-8)
 C-1615A (Ch. 16AY21) Tel. Rec. (Also see PCB 19—Set 132-1 and Model C-1615B—Set 124-8)
 C-1615B (Ch. 16AY28) Tel. Rec. (Also see PCB 19—Set 132-1 and Model C-1615B—Set 124-8)
 C-1616A (Ch. 16AY21) Tel. Rec. (Also see PCB 19—Set 132-1 and Model C-1616B—Set 124-8)
 C-1616B (Ch. 16AY28) Tel. Rec. (Also see PCB 19—Set 132-1 and Model C-1616B—Set 124-8)
 C-1714A (Ch. 17AY21) Tel. Rec. (See PCB 19—Set 132-1 and Model C-1715A—Set 124-8)
 C-1714B (Ch. 17AY21) Tel. Rec. (Also see PCB 19—Set 132-1 and Model C-1715A—Set 124-8)
 C-1715A (Ch. 17AY24) Tel. Rec. (Also see PCB 19—Set 132-1 and Model C-1716B—Set 124-8)
 C-1716A (Ch. 17AY24) Tel. Rec. (Also see PCB 19—Set 132-1 and Model C-1716B—Set 124-8)
 C-1717A (Ch. 17AY21) Tel. Rec. (Also see PCB 19—Set 132-1 and Model C-1718B—Set 124-8)
 C-1717B (Ch. 17AY21) Tel. Rec. (Also see PCB 19—Set 132-1 and Model C-1718B—Set 124-8)
 C-1718A (Ch. 17AY24) Tel. Rec. (Also see PCB 19—Set 132-1 and Model C-1718B—Set 124-8)
 C-1718B (Ch. 17AY21) Tel. Rec. (Also see PCB 19—Set 132-1 and Model C-1718B—Set 124-8)
 C-1719A (Ch. 17AY24) Tel. Rec. (See PCB 19—Set 132-1 and Model M-1711B—Set 124-8)
 C-2107A (Ch. 21T1) Tel. Rec. (Also see PCB 86—Set 230-1) 189-14
 M-2107a, iA, mA Tel. Rec. (See PCB 87—Set 230-1 and Model C-1735A—Set 189-14)
 M-2107A (Ch. 21T1) Tel. Rec. (Also see PCB 86—Set 230-1) 189-14
 M-2107b, iA, mA Tel. Rec. (See PCB 87—Set 230-1 and Model C-1735A—Set 189-14)
 M-2107B (Ch. 21T1) Tel. Rec. (See PCB 87—Set 230-1 and Model C-1735A—Set 189-14)
 M-2108, M-1106, M-1107 (Ch. 12AX26, 12AX27) Tel. Rec. 141-11
 M-1402, M-1403, M-1404 (Ch. 14AX21) Tel. Rec. 123-12
 M-1601 (Ch. 16AX23, 25, 26) Tel. Rec. 99-14
 M-1611A (Ch. 16AY21) Tel. Rec. (Also see PCB 19—Set 132-1) 124-8
 M-1612A (Ch. 16AY21) Tel. Rec. (Also see PCB 19—Set 132-1) 124-8
 M-1613A (Ch. 16AY21) Tel. Rec. (Also see PCB 19—Set 132-1) 124-8
 M-1613B (Ch. 16AY28) Tel. Rec. (Also see PCB 19—Set 132-1) 124-8
 M-1626 (Ch. 16AY21) Tel. Rec. 165-24
 M-1711A (Ch. 17AY24) Tel. Rec. (Also see PCB 19—Set 132-1) 124-8
 M-1712A (Ch. 17AY24) Tel. Rec. (Also see PCB 19—Set 132-1) 124-8
 M-1713A (Ch. 17AY24) Tel. Rec. (Also see PCB 19—Set 132-1) 124-8
 M-1725A (Ch. 17AY21) Tel. Rec. (See PCB 19—Set 132-1 and Model M-1711B—Set 124-8)
 M-1726A (Ch. 17AY21) Tel. Rec. (See PCB 19—Set 132-1 and Model M-1711B—Set 124-8)
 M-1733A (Ch. 17T1) Tel. Rec. (Also see PCB 87—Set 230-1) 189-14
 M-1733b, iA, mA (Ch. 17T1) Tel. Rec. (See PCB 87—Set 230-1 and Model C-1735A—Set 189-14)
 M-1734A (Ch. 17T1) Tel. Rec. (For TV Ch. See PCB 87—Set 230-1 and Model C-1735A—Set 189-14)
 M-2007A, M-2008A (Ch. 20AY21) Tel. Rec. (See PCB 43—Set 177-1 and Model C-2001A—Set 149-9)
 M-2101A (Ch. 21AY21) Tel. Rec. (See Model C-203A) 173-1A
 M-2107A (Ch. 21T1) Tel. Rec. (Also see PCB 86—Set 230-1) 189-14
 M-2107b, iA, mA Tel. Rec. (See PCB 87—Set 230-1 and Model C-1735A—Set 189-14)
 M-2107B (Ch. 21T1) Tel. Rec. (See PCB 87—Set 230-1 and Model C-1735A—Set 189-14)
 M-2131A (Ch. 21T1) Tel. Rec. 244-8
 PR-51, A (Ch. 4P12, A) 26-9
 P-201 Tel. Rec. (See Model 7DX21—Set 81-13)
 RC-1405 (Ch. 14AX21) Tel. Rec. (For TV Ch. only see Model C-1401—Set 123-12)
 RC-1618A (Ch. 16AY21) Tel. Rec. (Also see PCB 19—Set 132-1)
 RC-1619A (Ch. 16AY21) Tel. Rec. (Also see PCB 19—Set 132-1)
 RC-1619B (Ch. 16AY28) Tel. Rec. (Also see PCB 19—Set 132-1)
 RC-1718A (Ch. 17AY24) Tel. Rec. (See PCB 19—Set 132-1 and Model M-1711B—Set 124-8)
 RC-1718B (Ch. 17AY21) Tel. Rec. (Also see PCB 19—Set 132-1)
 RC-1720A (Ch. 17AY27) Tel. Rec. 147-9
 RC-2005A (Ch. 20AY21) Tel. Rec. (See PCB 43—Set 177-1 and Model C-2001A—Set 149-9)
 RC-2117A (Ch. 21T3) Tel. Rec. (Also see PCB 89—Set 233-1) 202-7
 RC-2121A, RC-2122A, RC-2123A (Ch. 21T3) Tel. Rec. (See PCB 89—Set 233-1 and Model C-2112A—Set 202-7)

RAYTHEON—Cont.

C-2006A (Ch. 20AY21) Tel. Rec. (Also see PCB 43—Set 177-1)
 C-2103A, C-2105A (Ch. 21AY21) Tel. Rec. 173-1A
 C-2108A (Ch. 21T1) Tel. Rec. (Also see PCB 87—Set 230-1 and Model C-2109A—Set 189-14)
 C-2109A (Ch. 21T2) Tel. Rec. (For TV Ch. See PCB 87—Set 230-1 and Model C-1735A—Set 189-14)
 C-2110A, C-2111A (Ch. 21T1) Tel. Rec. (Also see PCB 87—Set 230-1)
 C-2112A, C-2113A, C-2114A, C-2115A, C-2116A, C-2118A (Ch. 21T3) Tel. Rec. (Also see PCB 89—Set 233-1) 202-7
 C-2127A, C-2129A (Ch. 21T5) Tel. Rec. (See PCB 87—Set 230-1 and Model C-1735A—Set 189-14)
 C-2137A, C-2138A (Ch. 21T1) Tel. Rec. 244-8
 C-2401A, C-2402A (Ch. 24T3) Tel. Rec. 244-8
 FR81A, FR82A (Ch. 9AF25A) 232-6
 M701 (Ch. 10AX22) Tel. Rec. (Also see PCB 3—Set 105-1) 94-8
 M1101, M1103, M1105 (Ch. 12AX-22) Tel. Rec. (Also see PCB 3—Set 105-1) 94-8
 M-1105B, M-1106, M-1107 (Ch. 12AX26, 12AX27) Tel. Rec. 141-11
 M-1402, M-1403, M-1404 (Ch. 14AX21) Tel. Rec. 123-12
 M-1601 (Ch. 16AX23, 25, 26) Tel. Rec. 99-14
 M-1611A (Ch. 16AY21) Tel. Rec. (Also see PCB 19—Set 132-1) 124-8
 M-1612A (Ch. 16AY21) Tel. Rec. (Also see PCB 19—Set 132-1) 124-8
 M-1613A (Ch. 16AY21) Tel. Rec. (Also see PCB 19—Set 132-1) 124-8
 M-1613B (Ch. 16AY28) Tel. Rec. (Also see PCB 19—Set 132-1) 124-8
 M-1626 (Ch. 16AY21) Tel. Rec. 165-24
 M-1711A (Ch. 17AY24) Tel. Rec. (Also see PCB 19—Set 132-1) 124-8
 M-1712A (Ch. 17AY24) Tel. Rec. (Also see PCB 19—Set 132-1) 124-8
 M-1713A (Ch. 17AY24) Tel. Rec. (Also see PCB 19—Set 132-1) 124-8
 M-1725A (Ch. 17AY21) Tel. Rec. (See PCB 19—Set 132-1 and Model M-1711B—Set 124-8)
 M-1726A (Ch. 17AY21) Tel. Rec. (See PCB 19—Set 132-1 and Model M-1711B—Set 124-8)
 M-1733A (Ch. 17T1) Tel. Rec. (Also see PCB 87—Set 230-1) 189-14
 M-1733b, iA, mA (Ch. 17T1) Tel. Rec. (See PCB 87—Set 230-1 and Model C-1735A—Set 189-14)
 M-1734A (Ch. 17T1) Tel. Rec. (For TV Ch. See PCB 87—Set 230-1 and Model C-1735A—Set 189-14)
 M-2007A, M-2008A (Ch. 20AY21) Tel. Rec. (See PCB 43—Set 177-1 and Model C-2001A—Set 149-9)
 M-2101A (Ch. 21AY21) Tel. Rec. (See Model C-203A) 173-1A
 M-2107A (Ch. 21T1) Tel. Rec. (Also see PCB 86—Set 230-1) 189-14
 M-2107b, iA, mA Tel. Rec. (See PCB 87—Set 230-1 and Model C-1735A—Set 189-14)
 M-2107B (Ch. 21T1) Tel. Rec. (See PCB 87—Set 230-1 and Model C-1735A—Set 189-14)
 M-2131A (Ch. 21T1) Tel. Rec. 244-8
 PR-51, A (Ch. 4P12, A) 26-9
 P-201 Tel. Rec. (See Model 7DX21—Set 81-13)
 RC-1405 (Ch. 14AX21) Tel. Rec. (For TV Ch. only see Model C-1401—Set 123-12)
 RC-1618A (Ch. 16AY21) Tel. Rec. (Also see PCB 19—Set 132-1)
 RC-1619A (Ch. 16AY21) Tel. Rec. (Also see PCB 19—Set 132-1)
 RC-1619B (Ch. 16AY28) Tel. Rec. (Also see PCB 19—Set 132-1)
 RC-1718A (Ch. 17AY24) Tel. Rec. (See PCB 19—Set 132-1 and Model M-1711B—Set 124-8)
 RC-1718B (Ch. 17AY21) Tel. Rec. (Also see PCB 19—Set 132-1)
 RC-1720A (Ch. 17AY27) Tel. Rec. 147-9
 RC-2005A (Ch. 20AY21) Tel. Rec. (See PCB 43—Set 177-1 and Model C-2001A—Set 149-9)
 RC-2117A (Ch. 21T3) Tel. Rec. (Also see PCB 89—Set 233-1) 202-7
 RC-2121A, RC-2122A, RC-2123A (Ch. 21T3) Tel. Rec. (See PCB 89—Set 233-1 and Model C-2112A—Set 202-7)

RAYTHEON—Cont.

UC-1735A (Ch. 17T2) Tel. Rec. (For TV Ch. See PCB 87—Set 230-1 and Model C-1735A—Set 189-14, For UHF Tuner See Model UHF-100—Set 207-8)
 UC-1740A, UC-1742A (Ch. 17T5) Tel. Rec. (For TV Ch. See PCB 87—Set 230-1 and Model C-1735A—Set 189-14, For UHF Tuner See Model UHF-100—Set 207-8)
 UC-2109A, UC-2110A (Ch. 21T2) Tel. Rec. (For TV Ch. See PCB 87—Set 230-1 and Model C-1735A—Set 189-14, For UHF Tuner See Model UHF-100—Set 207-8)
 UC-2128A, UC-2130A (Ch. 21T6) Tel. Rec. (For TV Ch. See PCB 87—Set 230-1 and Model C-1735A—Set 189-14, For UHF Tuner See Model UHF-100—Set 207-8)
 UC-2139A, UC-2141A, UC-2142A, UC-2144A, UC-2145A (Ch. 21T8) Tel. Rec. (For TV Ch. See PCB 87

REGAL-Cont.

Table listing Regal models and their specifications, including 19C31, 19D36, 20C22, 20C22DX, etc.

REGENCY

Table listing Regency models, including RC-600 Tel. UHF Conv.

REMBRANDT

Table listing Rembrandt models, including 721, 1600, 1606-15, 1950 Tel. Rec.

REMNER

Table listing Remner models, including MP5-5-3, 5300B, 5100B1, 53001, etc.

REWARD

Table listing Reward models, including L-1A, PT-1A, 185T-1

REVERSE (See Recorder Listing)

ROLAND

Table listing Roland models, including 4T1, 5C1, 5C2, 5P2, 5P4, etc.

ROYAL Lee

Table listing Royal Lee models, including AN150, AN160, 20CP, etc.

SCOTT (E. H.)

Table listing Scott (E. H.) models, including 6111, 6111A, 6111B, 6111C, etc.

SCOTT (E. H.)-Cont.

Table listing Scott (E. H.) models, including 8217B, 9039, 8217B, TH, etc.

SCOTT (H. H.)

Table listing Scott (H. H.) models, including 111-B, 112-B, 113-B, etc.

SEARS-ROEBUCK

(See Allstate or Silvertone)

SEEBURG

(See Record Changer Listing)

SENTINEL

Table listing Sentinel models, including 1U-284CA, 1U-284I, 1U-284NA, etc.

SENTINEL-Cont.

Table listing Sentinel models, including 2841, 284NA, 284NI, 285P, etc.

SHERATON-Cont.

Table listing Sheraton models, including 21BD10, 21MC10, 21MD10, etc.

SHERATON-Cont.

Table listing Sheraton models, including 21BD10, 21MC10, 21MD10, etc.

SHERIDAN ELECTRONICS

(See Vogue)

SIGNAL

Table listing Signal models, including AF252, 141, 241, etc.

SILVERLINE (See General Instrument)

SILVERTONE (Also see Changer and Recorder Listing)

Table listing Silvertone models, including 1, 2, 5, 6, 10, 11, 15, 16, etc.

SILVERTONE-Cont.

Table listing Silvertone models, including 166-16, 167-16, 168-16, etc.

SILVERTONE

SILVERTONE—Cont.

2001, 2002 (Ch. 132.878) (See Model 1—Set 101-10)
2003, 2004, 2005, 2006 (Ch. 757-110)
2007 (Ch. 757.100)
2009, 2010, 2011, 2012, 2013 (Ch. 132.022)
2014, 2015, 2016 (Ch. 132.021)
2022 (Ch. 132.027)
2023, 2024, 2025, 2026, 2027 (Ch. 132.896-1) (See Model 10—Set 144-11)
2028 (Ch. 528.230)
2035A (Ch. 528.195, -1 -2)
2041 (Ch. 528.235)
2041 (Ch. 528.235-1) (See Model 2041—Set 208-11)
2056 (Ch. 132.026, -1, -2)
2060, 2061 (Ch. 101.861, -1)
2063, 2064 (Ch. 101.860, -1) (See Model 1058)
2068 (Ch. 100.202) (See Model 1066—Set 162-10)
2100 (Ch. 110.700-100, -104) Tel. Rec.
2100A (Ch. 110.817-1) Tel. Rec.
2101 (Ch. 447.023) Tel. Rec.
2105 (Ch. 132.024, -1, -2) Tel. Rec.
2105A (Ch. 132.024, -3) Tel. Rec.
2110A, 2111 (Ch. 528.631, -1, -2, -3, -4, -5)
2115 (Ch. 528.632A, -1, -2, -3, -5)
2158 (Ch. 528.631, -1, Ch. 528.632, -1, -2, -3, -4, -5, Ch. 528.632A, -1, -2, -3, -5)
2170 (Ch. 100.210, -1, -3) Tel. Rec.
2170A (Ch. 110.817-1) Tel. Rec.
2175 (Ch. 132.024, -1, -2) Tel. Rec.
2175A (Ch. 132.024, -3) Tel. Rec.
2185 (Ch. 132.024, 4) Tel. Rec.
2190 (Ch. 110.700-140) Tel. Rec.
2190A (Ch. 110.820-1) Tel. Rec.
2195 (Ch. 528.631, -1, Ch. 528.632, -1, -2, -3, -4, -5, Ch. 528.632A, -1, -2, -3, -5)
2195-21 (Ch. 100.208-1 and Radio Ch. 100.202-1) Tel. Rec. (See PCB 59—Set 193-1 and Model 1176-21—Set 165-12 for TV Ch. and Model 1066—Set 162-10 for Radio Ch.)
2200, 2202, 2203 (Ch. 528.229)
2210 (Ch. 132.880) (See Model 210—Set 109-12)
2215, 2217, 2218 (Ch. 528.238)
2225 (Ch. 528.233)
2243 (Ch. 137.914, -1, -2, -3)
2246 (Ch. 137.914, -1, -2, -3)
2276, 2277 (Ch. 456.150-18)
3001, 3002 (Ch. 132.054)
3004 (Ch. 757.130)
3007, 3008, 3009 (Ch. 757.120)
3025, 3026, 3027 (Ch. 132.066)
3032 (Ch. 528.252)
3035A (Ch. 528.195, -1 -2)
3040 (Ch. 528.253)
3041 (Ch. 528.235-1) (See Model 2041—Set 208-11)
3045, 3046 (Ch. 528.254)
3052, 3053 (Ch. 132.053)
3054, 3055 (Ch. 132.056)
3058, 3059 (Ch. 101.860-3)
3061, 3062 (Ch. 101.861-1) (See Model 2060—Set 203-9)
3063, 3064 (Ch. 101.860-3)
3067 (Ch. 101.860-3)
3100 (Ch. 110.817-1) Tel. Rec. (See Model 2100A—Set 217-15)
3100A (Ch. 110.817-1, -3) Tel. Rec. (See Model 2100A—Set 217-15)
3101 (Ch. 110.817-3) Tel. Rec. (See Model 2100A—Set 217-15)
3104A (Ch. 528.271, -4) Tel. Rec.
3105 (Ch. 132.024, -5, -6) Tel. Rec.
3106 (Ch. 132.045, -1, -2, -3, -4, -5) Tel. Rec. (Also see PCB 90—Set 235-1)
3109 (Ch. 528.264) Tel. Rec.
3110 (Ch. 528.248, -1, -2) Tel. Rec.
3110A (Ch. 528.242, -1) Tel. Rec.
3110B (Ch. 528.264-1, -2) Tel. Rec.
3112A (Ch. 528.256) Tel. Rec. (See Model 3112B—Set 227-12)

SILVERTONE—Cont.

3112B (Ch. 528.263, -1, -2) Tel. Rec.
3112C (Ch. 528.258) Tel. Rec.
3115 (Ch. 528.248, -1, -2) Tel. Rec.
3115A (Ch. 528.242, -1, -2) Tel. Rec.
3127 (Ch. 100.210, -1, -3) Tel. Rec.
3140 (Ch. 110.817-1, -3) Tel. Rec. (See Model 2100A—Set 217-15)
3145 (Ch. 132.024, -5, -6) Tel. Rec.
3146 (Ch. 132.045, -2, -3, -4, -5) Tel. Rec. (See PCB 90—Set 235-1 and Model 3106—Set 199-11)
3150 (Ch. 110.820-1, -3) Tel. Rec. (See Model 2100A—Set 217-15)
3150L (Ch. 528.264, -1, -2) Tel. Rec.
3151A (Ch. 528.256) Tel. Rec. (See Model 3151B—Set 227-12)
3151B, C (Ch. 528.263, -1, -2) Tel. Rec.
3160 (Ch. 528.248, -1, -2) Tel. Rec.
3160A (Ch. 528.242, -1, -2) Tel. Rec.
3170 (Ch. 528.239) Tel. Rec.
3170-B (Ch. 100.210, -1, -3) Tel. Rec.
3170C (Ch. 528.249, -1) Tel. Rec.
3170D (Ch. 528.261) Tel. Rec.
3171A (Ch. 528.247, -1) Tel. Rec.
3174 (Ch. 132.035-2) Tel. Rec.
3175 (Ch. 132.044) Tel. Rec.
3177 (Ch. 100.210, -1, -3) Tel. Rec.
3177A (Ch. 100.400) Tel. Rec.
3187 (Ch. 100.210, -1, -3) Tel. Rec.
3187A (Ch. 100.400) Tel. Rec.
3195 (Ch. 100.210-2 and Radio Ch. 100.202-1) Tel. Rec. (See PCB 91—Set 236-1 and Model 2130—Set 207-1 for TV Ch. and Model 1066—Set 162-10 for Radio Ch.)
3200 (Ch. 528.259)
3202, 3203 (Ch. 528.259)
3210 (Ch. 528.241)
3215 (Ch. 528.265)
3217 (Set 227-13)
3217 (Ch. 528.265)
3218 (Ch. 528.265) (See Model 3217—Set 227-13)
3276, 3277 (Ch. 456.150-61) Tel. Rec.
3376, 3377 (Ch. 456.200-111, -112, -113, -114, -115, -121, -122, -123, -124, -125) Tel. Rec.
4108 (Ch. 528.271) Tel. Rec.
4108A (Ch. 528.271, -1, -2, -3) Tel. Rec.
4111 (Ch. 528.264-1, -2) Tel. Rec.
4112 (Ch. 528.303, -1) Tel. Rec.
4113 (Ch. 528.263-1, -2) Tel. Rec.
4113A (Ch. 528.292-1) Tel. Rec.
4113B (Ch. 528.303, -1) Tel. Rec.
4114 (Ch. 528.264-2) Tel. Rec.
4115 (Ch. 528.270) Tel. Rec.
4116, 4117 (Ch. 528.266) Tel. Rec.
4118 (Ch. 528.263-1, -2) Tel. Rec.
4118B (Ch. 528.292-1, -2, -3) Tel. Rec.
4118C (Ch. 528.303, -1) Tel. Rec.
4119 (Ch. 528.263-2) Tel. Rec.
4119A (Ch. 528.303, -1) Tel. Rec.
4120 (Ch. 456.150, -2) Tel. Rec.
4125 (Ch. 528.271-1, -2, -3, -4) Tel. Rec.
4126 (Ch. 528.264-1, -2) Tel. Rec.
4127 (Ch. 528.263-1, -2) Tel. Rec.
4127A (Ch. 528.268) Tel. Rec.
4127C (Ch. 528.292, -1) Tel. Rec.
4127D (Ch. 528.303, -1) Tel. Rec.
4128 (Ch. 528.264-2) Tel. Rec.
4129 (Ch. 528.263-2) Tel. Rec.
4129A (Ch. 528.292, -1) Tel. Rec.
4129B (Ch. 528.303, -1) Tel. Rec.
4131 (Ch. 528.263-1) Tel. Rec.
4133 (Ch. 528.292-2, -3) Tel. Rec.
4135 (Ch. 528.292, -1, -3) Tel. Rec.
4139 (Ch. 528.270) Tel. Rec.
4140 (Ch. 528.247, -1) Tel. Rec.
4140D (Ch. 528.266-1) Tel. Rec.
4140E (Ch. 528.300, -1, -2, -3) Tel. Rec.
4143 (Ch. 528.247, -1) Tel. Rec.

SILVERTONE—Cont.

4143D (Ch. 528.266-1) Tel. Rec.
4145 (Ch. 528.247, -1) Tel. Rec.
4145D (Ch. 528.266-1) Tel. Rec.
4149 (Ch. 528.270) Tel. Rec.
4150 (Ch. 528.247, -1) Tel. Rec.
4150D (Ch. 528.286) Tel. Rec.
4150E (Ch. 528.260, -3) Tel. Rec.
4153 (Ch. 528.247, -1) Tel. Rec.
4153D (Ch. 528.286) Tel. Rec.
4153E (Ch. 528.300-3) Tel. Rec. (See Model 4140E—Set 245-6)
4155 (Ch. 528.247, -1) Tel. Rec.
4155D (Ch. 528.286) Tel. Rec.
4155E (Ch. 528.300-3, -1) Tel. Rec.
5113 (Ch. 528.303-1) Tel. Rec. (See Model 4118C—Set 245-6)
6002 (Ch. 132.818)
6011 (Ch. 132.816), 6012 (Ch. 132.816A)
6016 (Ch. 132.820)
6050 (Ch. 132.825-4)
6051 (Ch. 110.451), 6052 (Ch. 110.452)
6052A (Ch. 110.452, -1) (See Model 6051—Set 132-29)
6071 (Ch. 132.826-1)
6072 (Ch. 110.454)
6092 (Ch. 101.672-1B), 6093 (Ch. 101.672-1A)
6100 (Ch. 101.660-1A)
6104 (Ch. 101.660-1D) (See Model 6105—Set 7-26)
6105 (Ch. 101.622-2B)
6106A (Ch. 101.662-4E)
6111 (Ch. 101.662-3F)
6111A (Ch. 101.662-5F)
6200A (Ch. 101.800-3)
6200A (Ch. 101.800-1)
6203 (Ch. 101.800A) (See Model 6200A—Set 9-29)
6220, 6220A (Ch. 101.801, 101-801-1A)
6230 (Ch. 101.802)
6230A (Ch. 101.802-1)
6285A (Ch. 101.666-1B)
6286 (Ch. 528.6286, -1, -3)
6287 (Ch. 528.6287, -1, -3)
6290 (Ch. 101.677-8)
6293 (Ch. 528.6293-2)
6295 (Ch. 528.6295)
6385 (Ch. 139.150, Ch. 139.150-1)
6450 (Ch. 725.101-1) Tel. UHF Conv.
7020 (See Model 7021—Set 16-31)
7021 (Ch. 101.807, 101.807A)
7025 (Ch. 132.807-2)
7034 (Ch. 101.808)
7070 (Ch. 101.817)
7080 (Ch. 101.809)
7080, 7080A (Ch. 101.809-2)
8070 (Ch. 101.817-1A) (See Model 7070—Set 30-26)
8072 (Ch. 101.834)
8073 (Ch. 135.243)
8080 (Ch. 101.852)
8083, 8083A (Ch. 101.809-1A)
8084, 8084A (Ch. 101.809-1B)
8086 (Ch. 101.814-5C)
8086A, 8086B (Ch. 101.814-6C)
7085 (Ch. 101.814)
7086 (Ch. 110.466)
7090 (Ch. 101.810)
7095 (Ch. 101.826) (See Model 7115—Set 16-31)
7100 (Ch. 101.811)
7102 (Ch. 101.814-1A)
7103 (Ch. 101.466-1)
7111 (Ch. 434.140)
7115 (Ch. 101.825), 7116 (Ch. 101.825-1A), 7117 (Ch. 101-825-1B)
7119 (Ch. 101.825-2C)
7145 (Ch. 436.200)
7148 (Ch. 431.188), 7148A (Ch. 431.188-1)
7152 (Ch. 109.626)
7153 (Ch. 109.627)
7165 (Ch. 101.823-A, 1A)
7166 (Ch. 101.823, 101.823-1)
7210 (Ch. 101.820)
7220 (Ch. 101.801-7C) (See Model 6220—Set 9-30)
7226 (Ch. 101.819A)
7230 (Ch. 101.802-2A) (See Model 6230—Set 11-21)
7300 (Ch. 435.240)
7350 (Ch. 435.241)
7353 (See Model 7350—Set 38-22)
8000 (Ch. 132.838)
8003 (Ch. 132.818-1)
8004 (See Model 8003—Set 53-22)
8005 (Ch. 132.839)
8011 (See Model 8010—Set 40-21)
8020 (Ch. 132.841)
8021 (Ch. 132.868)
8024, 8025 (Ch. 478.206-1)
8050 (Ch. 101.813)
8051 (Ch. 101.829)
8052 (Ch. 101.808-1C)
8053 (Ch. 101.808-D) (See Model 8052—Set 68-15)
8090 (Ch. 101.821)
8097 (Ch. 101.825-3G) (See Model 8115—Set 62-18)
8097A (Ch. 101.825-4)
8100 (Ch. 101.829)
8101, 8101A, 8101B, 8101C (Ch. 101.809-3C)

SILVERTONE—Cont.

8102 (Ch. 101.814-2B)
8102A (Ch. 101.814-3B)
8102B (Ch. 101.814-2B)
8103 (Ch. 110.473)
8104 (See Model 8078—Set 61-18)
8105, 8105A (Ch. 101.833)
8106, A (Ch. 101.833-1A) (See Model 8105—Set 35-20)
8107A, 8108, 8108A (Ch. 101.851), 8109 (Ch. 101.851-1)
8112, 8113 (Ch. 101.851) (See Model 8112C—Set 41-20)
8115 (Ch. 101.825-3D)
8115, A, B, C (Ch. 101.825-4)
8115D (Ch. 101.825-4) (See Model 8115A—Set 62-18)
8117 (Ch. 101.825-3E)
8118 (Ch. 101.825-3F)
8118 A, B, C (Ch. 101.825-4)
8118D (Ch. 101.825-4) (See Model 8118A—Set 62-18)
8124, 8125, 8126 (Ch. 101.831A), 101.831-1 (See Model 8127—Set 41-20)
8127, A, B, C (Ch. 101.831), 8128, A, B, C (Ch. 101.831), Wire Recorder Amp. (Ch. 101-723)
8127C (Ch. 101.831A and Wire Recorder Amp. 101.773) (See Model 8127—Set 41-20)
8130 Tel. Rec.
8132 (Ch. 101.854) Tel. Rec.
8133 (Ch. 101.829-1, Ch. 101.846)
8140 (Ch. 431.199)
8145 (Ch. 109.631)
8148 (Ch. 109.632)
8149 (Ch. 109.633)
8150 (Ch. 109.634)
8152 (Ch. 101.665-1) (See Model 8151—Set 42-22)
8153 (Ch. 109.635), 8153A (Ch. 109.635-1)
8155 (Ch. 463.155)
8160 (Ch. 109.636A)
8168 (Ch. 101.638)
8169 (Ch. 109.638) (See Model 8168—Set 46-23)
8200 (Ch. 101.800-2B) (See Model 6200A—Set 65-12)
8201 (See Model 6200A—Set 65-12)
8210 (Ch. 101.820-1A)
8220, 8221 (Ch. 101.801-3D) (See Model 6220—Set 9-30)
8222 (See Model 6220—Set 9-30)
8230 (Ch. 101.835)
8231 (See Model 6230—Set 59-18)
8240 (Ch. 101.823-8) (See Model 7165—Set 10-29)
8270 (Ch. 101.822), 8270A (Ch. 101.822A)
9000 (Ch. 132.857)
9025, 9026 (Ch. 132.858)
9027 (Ch. 132.871)
9054 (Ch. 101.849)
9073, 9073A (Ch. 135.244), 9073B (Ch. 135.244-1)
9073C (Ch. 135.243-1) (See Model 9073—Set 83-10)
9082 (Ch. 135.244-1)
9101 (Ch. 101.809-3C) (See Model 7080—Set 58-20)
9102 (See Model 7080—Set 58-20)
9105 (Ch. 132.875)
9107A (Ch. 101.851-1) (See Model 8107A—Set 64-10)
9111 (Ch. 110.499) Tel. Rec. (See Model 9123—Set 79-16)
9112 (Ch. 110.499-1) Tel. Rec. (See Model 9124—Set 79-16)
9113 (Ch. 110.499) Tel. Rec. (See Model 9123—Set 79-16)
9114 (Ch. 110.499-1) Tel. Rec. (See Model 9124—Set 79-16)
9115 (Ch. 478.224), 9116 (Ch. 478.221) Tel. Rec.
9116 (Ch. 478.221) Tel. Rec.
9119, 9120 (Ch. 101.865) Tel. Rec.
9120A (Ch. 101.862-1) Tel. Rec.
9121 (Ch. 101.867) Tel. Rec.
9122 (Ch. 101.864) (See Model 8132—Set 66-15)
9124A (Ch. 101.868) Tel. Rec.
9123 (Ch. 110.499) Tel. Rec.
9124 (Ch. 110.499-1) Tel. Rec.
9125 (Ch. 478.252) Tel. Rec.
9125A (Ch. 478.253) Tel. Rec.
9125B (Ch. 478.253-1) Tel. Rec.
9126 (Ch. 110.499-2) Tel. Rec.
9127 (Ch. 100.499-2) Tel. Rec. (See Model 9126—Set 79-16)
9128A (Ch. 101.868) Tel. Rec.
9129 (Ch. 110.499-1) Tel. Rec. (See Model 9123—Set 79-16)
9130 (Ch. 110.499-2) Tel. Rec. (See Model 9124—Set 79-16)
9131 (Ch. 478.210) Tel. Rec.
9132 (Ch. 110.499-1) Tel. Rec. (See Model 9124—Set 79-16)
9133, 9134 (Ch. 101.866 and Radio Ch. 101.859) Tel. Rec.
9139, 9140 (Ch. 110.499-1) Tel. Rec. (See Model 9124—Set 79-16)
915 (Ch. 435.417)
9161 (Ch. 548.358)
9260 (Ch. 101.850)
9270 (Ch. 547.245)
9280 (Ch. 528.168)
Ch. 100.043 (See Model 133)
Ch. 100.107 (See Model 133)
Ch. 100.107-1 (See Model 149)
Ch. 100.111 (See Model 143A)
Ch. 100.112 (See Model 161-16)
Ch. 100.115 (See Model 142)
Ch. 100.120 (See Model 165-16)
Ch. 100.201 (See Model 69)
Ch. 100.202 (See Model 1066)
Ch. 100.202-1 (See Model 2195-21 or 3195)

SILVERTONE—Cont.

Ch. 100.208 (See Model 1176-21)
Ch. 100.209-1 (See Model 2195-21)
Ch. 100.208-1 (See Model 2195-C)
Ch. 100.210, -1 (See Model 2130)
Ch. 100.210-2 (See Model 3195)
Ch. 100.210-3 (See Model 3130)
Ch. 100.400 (See Model 3177A)
Ch. 100.959 (See Model 142)
Ch. 101.660-1A (See Model 6100)
Ch. 101.662-2B (See Model 6105)
Ch. 101.662-2D (See Model 6105)
Ch. 101.662-4C (See Model 6111)
Ch. 101.662-5F (See Model 6111A)
Ch. 101.666-1B (See Model 6285A)
Ch. 101.672-1A (See Model 6093)
Ch. 101.672-1B (See Model 6092)
Ch. 101.677B (See Model 6290)
Ch. 101.773 (See Model 8127)
Ch. 101.800-1, -1A (See Model 6200A, Ch. 101.800-1, -1A)
Ch. 101.800-3 (See Model 6200A, Ch. 101.800-3)
Ch. 101.801, -1A (See Model 6230)
Ch. 101.802, -1 (See Model 7050)
Ch. 101.807, A (See Model 7021)
Ch. 101.808 (See Model 7034)
Ch. 101.808-1C (See Model 8052)
Ch. 101.808-1D (See Model 8053)
Ch. 101.809 (See Model 7080, Ch. 101.809)
Ch. 101.809-1A (See Model 8083)
Ch. 101.809-1B (See Model 8084)
Ch. 101.809-2 (See Model 7080, Ch. 101.809-2)
Ch. 101.809-3C (See Model 8101)
Ch. 101.810 (See Model 7090)
Ch. 101.811 (See Model 7100)
Ch. 101.813 (See Model 8050)
Ch. 101.814 (See Model 7085)
Ch. 101.814-1A (See Model 7102)
Ch. 101.814-2B (See Model 8102A)
Ch. 101.814-3B (See Model 8102A)
Ch. 101.814-5C (See Model 8086)
Ch. 101.814-6C (See Model 8086A)
Ch. 101.817 (See Model 7070)
Ch. 101.819A (See Model 7226)
Ch. 101.820 (See Model 7210)
Ch. 101.821 (See Model 8090)
Ch. 101.822-3G (See Model 8097)
Ch. 101.822A (See Model 8270A)
Ch. 101.823, -1 (See Model 7166)
Ch. 101.823A, -1A (See Model 7165)
Ch. 101.825 (See Model 7115)
Ch. 101.825-1 (See Model 7116)
Ch. 101.825-1B (See Model 7117)
Ch. 101.825-2C (See Model 7119)
Ch. 101.825-2C (See Model 7119)
Ch. 101.825-3E (See Model 8115)
Ch. 101.825-3F (See Model 8118)
Ch. 101.825-3G (See Model 8097)
Ch. 101.825-4 (See Model 8097A)
Ch. 101.829 (See Model 8100)
Ch. 101.829-1 (See Model 8133)
Ch. 101.831 (See Model 8128)
Ch. 101.831A (See Model 8124)
Ch. 101.831-1 (See Model 8124)
Ch. 101.833 (See Model 8105)
Ch. 101.834 (See Model 8072)
Ch. 101.835 (See Model 8230)
Ch. 101.839 (See Model 8351)
Ch. 101.846 (See Model 9054)
Ch. 101.849 (See Model 9054)
Ch. 101.850 (See Model 9260)
Ch. 101.851 (See Model 8107A)
Ch. 101.851-1 (See Model 8109)
Ch. 101.852 (See Model 8080)
Ch. 101.854 (See Model 8132)
Ch. 101.859 (See Model 8097)
Ch. 101.859-1 (See Model 67)
Ch. 101.859-2 (See Model 64)
Ch. 101.860 (See Model 1058)
Ch. 101.860-3 (See Model 3058)
Ch. 101.861, -1 (See Model 2060)
Ch. 101.864 (See Model 9124)
Ch. 101.865 (See Model 9119)
Ch. 101.865-1 (See Model 9120A)
Ch. 101.866 (See Model 9133)
Ch. 101.867 (See Model 9121)
Ch. 101.868 (See Model 1122A)
Ch. 101.869 (See Model 7153)
Ch. 101.869-2 (See Model 7153)
Ch. 101.869-3 (See Model 8145)
Ch. 101.869-4 (See Model 8148)
Ch. 101.869-5 (See Model 8149)
Ch. 101.869-6 (See Model 8150)
Ch. 101.869-7 (See Model 8153)
Ch. 101.869-8 (See Model 8153A)
Ch. 101.869-9 (See Model 8160)
Ch. 101.869-10 (See Model 8160A)
Ch. 101.869-11 (See Model 8168)
Ch. 101.431 (See Model 6051)
Ch. 101.432 (See Model 6052)
Ch. 101.454 (See Model 6072)
Ch. 101.466 (See Model 7086)
Ch. 101.466-1 (See Model 7103)
Ch. 101.473 (See Model 8103)
Ch. 101.499 (See Model 9123)
Ch. 101.499-1 (See Model 9124)
Ch. 101.499-2 (See Model 9126)
Ch. 101.700 (See Model 111)
Ch. 101.700-1 (See Model 116)
Ch. 101.700-2 (See Model 134)
Ch. 101.700-10 (See Model 116)
Ch. 101.700-11 (See Model 116)
Ch. 101.700-40 (See Model 177-19)
Ch. 101.700-90 (See Model 1116-16)
Ch. 101.700-96 (See Model 1117-17)
Ch. 101.700-100 (See Model 1117-17)
Ch. 101.700-120 (See Model 1181-20)
Ch. 101.700-140 (See Model 1145-20)
Ch. 101.700-150 (See Model 1183-21)
Ch. 101.702-10, -50 (See Model 1171-17)
Ch. 101.817-1 (See Model 2100A)
Ch. 101.817-3 (See Model 2100A)
Ch. 101.820-1 (See Model 3150)
Ch. 101.820-3 (See Model 1052)
Ch. 101.820-11 (See Model 1053A)
Ch. 101.820-12 (See Model 1054)

NOTE: PCB denotes Production Change Bulletin

SILVERTONE—Cont.

Ch. 132.012-1 (See Model 1054A)
Ch. 132.021 (See Model 2014)
Ch. 132.022 (See Model 2009)
Ch. 132.024, -1, -2 (See Model 2105)
Ch. 132.024-3 (See Model 2105A)
Ch. 132.024-4 (See Model 2022)
Ch. 132.024-4 (See Model 2145B)
Ch. 132.024-5, -6 (See Model 3105)
Ch. 132.024-31 (See Model 2105A)
Ch. 132.026-3 (See Model 2056)
Ch. 132.027 (See Model 2022)
Ch. 132.035 (See Model 2174)
Ch. 132.035-2 (See Model 3174)
Ch. 132.044 (See Model 3175)
Ch. 132.045, -1, -2, -3, -4, -5 (See Model 3106)
Ch. 132.053 (See Model 3052)
Ch. 132.054 (See Model 3001)
Ch. 132.056 (See Model 3054)
Ch. 132.066 (See Model 3025)
Ch. 132.807-2 (See Model 7025)
Ch. 132.816 (See Model 6011)
Ch. 132.816A (See Model 6012)
Ch. 132.818 (See Model 6002A)
Ch. 132.818-1 (See Model 8003)
Ch. 132.820 (See Model 6016)
Ch. 132.825-4 (See Model 6050)
Ch. 132.826-1 (See Model 6071)
Ch. 132.838 (See Model 8005)
Ch. 132.839 (See Model 8005)
Ch. 132.840 (See Model 8010)
Ch. 132.841 (See Model 8020)
Ch. 132.858 (See Model 9005)
Ch. 132.868 (See Model 8021)
Ch. 132.871 (See Model 9022)
Ch. 132.875 (See Model 9105)
Ch. 132.877 (See Model 18)
Ch. 132.878 (See Model 1)
Ch. 132.880 (See Model 210)
Ch. 132.881 (See Model 5)
Ch. 132.884, -1, -2 (See Model 15)
Ch. 132.887 (See Model 4)
Ch. 132.888 (See Model 54)
Ch. 132.889, -1 (See Model 106, Ch. 132.889-1)
Ch. 132.889, -2 (See Model 106, Ch. 132.889-2)
Ch. 132.890 (See Model 179-16)
Ch. 132.896 (See Model 10)
Ch. 132.896-1 (See Model 2023)
Ch. 134.111 (See Model 72)
Ch. 135.243 (See Model 8073)
Ch. 135.243-1 (See Model 9073C)
Ch. 135.244 (See Model 9073)
Ch. 135.244-1 (See Model 9073B)
Ch. 135.245 (See Model 41)
Ch. 137.906 (See Model 246)
Ch. 137.914, -1, -2, -3 (See Model 2243)
Ch. 139.150, -1 (See Model 6685)
Ch. 185.706 (See Model 3012)
Ch. 319.190 (See Model 1301)
Ch. 319.200 (See Model 1300)
Ch. 319.200-1 (See Model 1300-1)
Ch. 431.188 (See Model 7148)
Ch. 431.188-1 (See Model 7148A)
Ch. 431.199 (See Model 8124)
Ch. 431.202 (See Model 8130)
Ch. 434.140 (See Model 7111)
Ch. 435.240 (See Model 7300)
Ch. 435.410 (See Model 7350)
Ch. 435.417 (See Model 9153)
Ch. 436.200 (See Model 7145)
Ch. 456.150 (See Model 1260)
Ch. 456.150-1 (See Model 1268-21)
Ch. 456.150-2 (See Model 1260)
Ch. 456.150-14, -18 (See Model 2276)
Ch. 456.150-61 (See Model 3276)
Ch. 456.200-111, -112, -113, -114, -115, -121, -122, -123, -124, -125 (See Model 3326)
Ch. 463.155 (See Model 8155)
Ch. 479.206-1 (See Model 8024)
Ch. 479.210 (See Model 9131)
Ch. 479.221 (See Model 9116)
Ch. 479.224 (See Model 9115)
Ch. 479.238 (See Model 25)
Ch. 479.240 (See Model 144)
Ch. 479.252 (See Model 9124)
Ch. 479.253 (See Model 9125A)
Ch. 479.253-1 (See Model 9125B)
Ch. 479.257 (See Model 125)
Ch. 479.257-1 (See Model 125B)
Ch. 479.289 (See Model 112)
Ch. 479.302 (See Model 163-16)
Ch. 479.303, A (See Model 110)
Ch. 479.309 (See Model 159)
Ch. 479.311 (See Model 120)
Ch. 479.312 (See Model 144)
Ch. 479.313 (See Model 164-14)
Ch. 479.319 (See Model 163-16)
Ch. 479.338 (See Model 150-14)
Ch. 479.339 (See Model 166-16)
Ch. 479.339-A (See Model 166-17)
Ch. 479.361, A (See Model 1150-14)
Ch. 488.237 (See Model 237)
Ch. 528.168 (See Model 9280)
Ch. 528.171-1 (See Model 225)
Ch. 528.173 (See Model 220)
Ch. 528.174 (See Model 215)
Ch. 528.194 (See Model 1040)
Ch. 528.195, -1, -2 (See Model 1035)
Ch. 528.196 (See Model 1032)
Ch. 528.210, -1 (See Model 1017)
Ch. 528.219 (See Model 1038)
Ch. 528.229 (See Model 2200)
Ch. 528.230 (See Model 2028)
Ch. 528.233 (See Model 2225)
Ch. 528.235 (See Model 2041)
Ch. 528.238 (See Model 2215)
Ch. 528.239 (See Model 3170)
Ch. 528.241 (See Model 3210)
Ch. 528.242, -1, -2 (See Model 3110A)
Ch. 528.247, -1 (See Model 3171A)
Ch. 528.248, -1, -2 (See Model 3110)
Ch. 528.249, -1 (See Model 3170C)
Ch. 528.252 (See Model 3032)
Ch. 528.253 (See Model 3040)
Ch. 528.254 (See Model 3045)
Ch. 528.256 (See Model 3112A)
Ch. 528.258 (See Model 3112C)

SILVERTONE—Cont.

Ch. 528.259 (See Model 3200)
Ch. 528.261 (See Model 3170D)
Ch. 528.263, -1, -2 (See Model 3112B)
Ch. 528.264, -1, -2 (See Model 3108)
Ch. 528.265 (See Model 3217)
Ch. 528.266 (See Model 4115)
Ch. 528.266-1 (See Model 4140D)
Ch. 528.268 (See Model 4127A)
Ch. 528.270 (See Model 4115)
Ch. 528.271, -1, -2, -3, -4 (See Model 4108A)
Ch. 528.286 (See Model 4150D)
Ch. 528.292, -1, -2, -3 (See Model 4118)
Ch. 528.300, -1, -2, -3 (See Model 4140E)
Ch. 528.303, -1 (See Model 4112)
Ch. 528.630, -1 (See Model 151-16)
Ch. 528.631 (See Model 1184-20)
Ch. 528.631, -1 (See Model 2110A)
Ch. 528.632, -1, -2, -3, -4, -5 (See Model 2110A)
Ch. 528.632A, -1, -2, -3, -5 (See Model 2110A)
Ch. 528.6286, -1, -3 (See Model 6286)
Ch. 528.6287, -1, -3 (See Model 6287)
Ch. 528.6293-2 (See Model 6293)
Ch. 528.6295 (See Model 6295)
Ch. 547.245 (See Model 9270)
Ch. 548.358 (See Model 9161)
Ch. 548.358-1 (See Model 245)
Ch. 548.360-1 (See Model 239)
Ch. 548.361 (See Model 239)
Ch. 548.363 (See Model 33)
Ch. 549.100 (See Model 101)
Ch. 549.100-1 (See Model 101A)
Ch. 549.100-3 (See Model 102A)
Ch. 549.100-4 (See Model 166-12)
Ch. 549.100-5, -6, -7, -8, -9 [See Model 175-16]
Ch. 549.102, -2 (See Model 169-16)
Ch. 725.101-1 (See Model 6950)
Ch. 737.100 (See Model 2007)
Ch. 737.110 (See Model 2008)
Ch. 757.120 (See Model 3007)
Ch. 757.130 (See Model 3004)
SIMPLON
CA-5 23-27
WV2 17-30
SKY KNIGHT (See Air Knight)
SKYRIDER (See Hallicrafters)
SKYROVER
N5-RD-250 (9022-N), N5-RD-251 (9022-H) 6-31
N5-RD295 (Ch. 5A7) 21-30
SKY WEIGHT
818 23-30
824 13-13
SONOGRAPH
BL100 122-10
BW100 (See Model BL100—Set 122-10)
SONORA
RB-176 5-31
RBU-207 (See Model RBU-176—Set 2-31)
RCU-208 5-30
RDU-209 3-29
RET-210 24-24
RGMF-212, RGMF-230 27-26
RKRU-215 (Ch. RKRU) 9-31
RMR-219 19-28
RMR-220, RMR-245 (See Model RMR-219—Set 19-28)
RQU-222 8-23
RWFU-238 23-24
RX-223 19-29
WAV-243 27-27
WBRU-239 32-23
WCU-246 36-22
WDU-233 25-27
WDU-249 37-20
WU-262 33-28
WGU-241, WGFU-242 26-16
WJU-252 36-23
WKRU-254A 34-20
WLRU-219A 37-21
WLRU-220A (See Model WLRU-219A—Set 37-21)
WLRU-245A (See Model WLRU-219A—Set 37-21)
YB-299 112-9
100 41-21
101 48-24
102 53-23
103 109-13
172 (See Model 171—Set 109-13)
302, 303 Tel. Rec. 97A-13
305 Tel. Rec. 174-11
306 108-11
324, 324, 325 Tel. Rec. 17-11
227A, 328A 249-16
332 Tel. Rec. 174-11
335, 336 250-19
341 251-16
348A 249-16
349 251-16
350, 351 Tel. Rec. 173-13
352 Tel. Rec. 182-12
356 251-16
366A 249-16
389, 390 245-7
401 47-21
402A (See Model RMR-219—Set 19-28)
402F (See Model WLRU-219A—Set 37-21)
413, 414, 415, 416 Tel. Rec. (For TV, Only See Model 421—Set 221-10)
421, 422, 423, 424, 425, 426, 428, 429 Tel. Rec. 104-11
464, 465, 466 249-17
470A 249-16

SOUND, INC.

"Intersound" 7-27
MB6P3, MB6PA, MB6P30, MB6R4 35-21
MB7E3 28-31
MB7E8 26-24
SR2 28-32
SPARKS-WITHINGTON (See Sparton)
SPARTON (Also see Record Changer Listing)
4AW17 (Ch. 417) 50-18
4AW17-A (Ch. 417A) 49-22
5A006, 5A106 (See Model 5A006—Set 4-17) 30-29
5A116 (Ch. 5-16) 5-17
5AW26-PS (Ch. 5-26-PS) 5-17
5AW06 (Ch. 5-06) 4-17
5AW16 (Ch. 5-16) 30-29
6A006 (Ch. 6-06) 34-21
6AW26 (See Model 6AW26PA—Set 4-17) 25-33
6AW26PA (Ch. PC5-6-26) 15-33
6-66A (Ch. 6-66A) 51-21
7AM46 (Ch. 7-46) 1-31
7AM46PA, 7BAM46PA, 7BAM46PA 1-31
8AM46 (Ch. 8-46) 1-31
10AB76-PA, 10AM76-PA, 10BM76-PA (See Model 10BW76-PA—Set 15-34) 15-34
10BW76-PA (Ch. 10-76PA) 15-34
100, 101 (Ch. 5A7) 38-23
102, 103, 104 (See Model 100—Set 38-23) 57-19
121 (Ch. 819) 57-19
122 (See Model 121—Set 57-19) 130, 132, 133, 139 (Ch. 5A10) 94-10
141 (See Model 121—Set 57-19) 92-6
141A (Ch. 8110) 126-12
141XX, 142XX (Ch. 8W10) 126-12
142 (See Model 121—Set 57-19) 150, 151, 152, 155 (Ch. 4E10) 91-12
230 (Ch. 5A10, A) 210-10
232 (Ch. 5A10, A) 210-10
239 (Ch. 5A10, A) 210-10
301, 305, 309 (Ch. 4E3) 222-13
320C, 321C (Ch. 5B3C) 237-10
325C (Ch. 5B3C) 237-10
329C (Ch. 5B3C) 237-10
342, 343, 347 (Ch. 5C3) 220-9
350, 351 (Ch. 613) 197-12
1000, 1001, 1003 (Ch. 1217) 60-18
1005, 1006, 1007, 1008 (Ch. 8-57) 29-25
1010 (Ch. 717) 35-22
1015 (See Model 10BW76PA—Set 15-34) 1020, 1021, 1023 60-18
1030, 1030A (Ch. 618) 37-22
1031, A (See Model 1030—Set 22) 1035, 1035A, 1036, 1036A, 1037, 1037A, 1039, 1040, 1041 (Ch. 918) 62-19
1040XX, 1041XX (Ch. 8W10) 126-12
1051, 1052 (Ch. 4B9) 58-21
1058, 1059, 1060, 1061, 1062 (Ch. 819) 57-19
1071 (See Model 121—Set 57-19) 1072 (Ch. 819) 57-19
1080 (Ch. 918A) (See Model 4900-TV—Set 64-11) 1080A (Ch. 8110) (See Model 141A—Set 92-6) 1081 (Ch. 918A) (See Model 4900-TV—Set 64-11) 1081A (Ch. 8110) (See Model 141A—Set 92-6) 1085, 1086 (Ch. 8W10) 126-12
1090, 1091 (Ch. 8W10) 126-12
1210, 1211 (Ch. 8W10) (See Model 141XX—Set 126-12) 1300, 1301 (Ch. 613) 197-12
4900TV (Ch. 24TV9C, 3TV9C, 918A) Tel. Rec. 64-11
4916, 4917, 4918 (Ch. 24T110, 3T110, 6510) Tel. Rec. 164-9
4920, 4921, 4922 (Ch. 24T10) Tel. Rec. 164-9
4935 Tel. Rec. 183-14
4937TV, 4940TV, 4941TV 1-11
24TV9, 3TV9TV Tel. Rec. 64-11
4942 (Ch. 23TC10) Tel. Rec. 133-1A
4944, 4945 (Ch. 3T810, 24T810) Tel. Rec. 86-10
4951, 4952 (See Model 4900TV—Set 64-11) 4954 (Ch. 23TC10) Tel. Rec. (See Model 4935) 133-1A
4960 (Ch. 23TC10) Tel. Rec. 133-1A
4964, 4965 (Ch. 23T810) Tel. Rec. 157-11
4970, 4971, 4972 (Ch. 8510) 92-6
5002, 5003 (Ch. 23TD10) Tel. Rec. 102-13
5006, 5007 (Ch. 23TD10) Tel. Rec. 102-13
5006X (Ch. 25TK10A) Tel. Rec. 121-13
5007X (Ch. 25TK10A) Tel. Rec. 121-13
5010, 5011 (Ch. 19TS10, A) Tel. Rec. 104-11
5014, 5015 (Ch. 19TS10, A) Tel. Rec. 104-11
5025 (Ch. 2655160) Tel. Rec. 128-13
5025BA Tel. Rec. See PCB 22—Set 138-1 and Model 5025—Set 128-13) 5026 Tel. Rec. 128-13
5029, 5030 (Ch. 265D160) Tel. Rec. 128-13
5035, 5036, 5037 (Ch. 2655160) Tel. Rec. 128-13
5052 (Ch. 24TR10, 3TR10) Tel. Rec. 97A-13
5056, 5057 (Ch. 19TS10, A) Tel. Rec. 5342A—Set 210-11) 5064, 5065 (Ch. 23T810) Tel. Rec. 157-11

SPARTON—Cont.

5068, 5069 (Ch. 24TV9C) Tel. Rec. (See Model 4900TV—Set 64-11) 5071, 5072 (Ch. 19TS10, A) Tel. Rec. 104-11
5075BA Tel. Rec. (See PCB 22—Set 138-1 and Model 5025—Set 128-13) 5076 (Ch. 2655160, B) Tel. Rec. 128-13
5076BA Tel. Rec. (See PCB 22—Set 138-1 and Model 5076—Set 128-13) 5076BB Tel. Rec. 128-13
5077 Tel. Rec. 128-13
5077BA Tel. Rec. (See PCB 22—Set 138-1 and Model 5077—Set 128-13) 5078 Tel. Rec. 128-13
5078B Tel. Rec. 128-13
5079 Tel. Rec. 128-13
5079B Tel. Rec. (See PCB 22—Set 138-1 and Model 5079—Set 128-13) 5080 Tel. Rec. 128-13
5080C Tel. Rec. (See PCB 22—Set 138-1 and Model 5080—Set 128-13) 5082, 5083 (Ch. 26SD160, 26SD170) Tel. Rec. (For TV Ch. see Set 128-13; for Radio Ch. see Model 141XX—Set 126-12) 5082, 5089, 5090 (Ch. 26SD160, 26SD170 and Radio Ch. 8W10) (For TV Ch. see Set 128-13; for Radio Ch. see Model 141XX—Set 126-12) 5101, 5102, 5103 (Ch. 2655170, P) Tel. Rec. (See PCB 22—Set 138-1 and Model 5025—Set 128-13) 5104, 5105 (Ch. 2655170D, P) Tel. Rec. (See PCB 22—Set 138-1 and Model 5025—Set 128-13) 5152, 5153, 5154 (Ch. 2655170, P) Tel. Rec. (See PCB 22—Set 138-1 and Model 5025—Set 128-13) 5155, 5156, 5157 (Ch. 26SD170X, XP) Tel. Rec. (See PCB 22—Set 138-1 and Model 5025—Set 128-13) 5158 (Ch. 26SD170, P) Tel. Rec. (See PCB 22—Set 138-1 and Model 5025—Set 128-13) 5165X, 5166X (Ch. 26SD171) Tel. Rec. 166-13
5170, 5171 (Ch. 25SD201, 25D201) Tel. Rec. (For TV Ch. see PCB 22—Set 138-1 and Model 5025—Set 128-13; for Radio Ch. see Model 141XX—Set 126-12) 5175X (Ch. 26SD171) Tel. Rec. 166-13
5178X (Ch. 26SD171) Tel. Rec. 166-13
5182, 5183, 5188, 5189 (Ch. 26SD170, P and Radio Ch. 8W10) Tel. Rec. (For TV Ch. see PCB 22—Set 138-1 and Model 5025—Set 128-13; for Radio Ch. see Model 141XX—Set 126-12) 5191, 5192 (Ch. 25SD201, 25D201) Tel. Rec. (See Model 5170—Set 147-11) 5207, 5208 (Ch. 2655172, A) Tel. Rec. 167-14
5210 (Ch. 2655172B) Tel. Rec. 167-14
5212 (Ch. 215172) Tel. Rec. 174-12
5220 (Ch. 26SD172C) Tel. Rec. 167-14
5225, 5226 (Ch. 26SD172C) Tel. Rec. 167-14
5240, 5241 (Ch. 215212) Tel. Rec. 201-10
5250, 5252, 5253 (Ch. 215172) Tel. Rec. 174-12
5262, 5263 (Ch. 2655172, A) Tel. Rec. 167-14
5265 (Ch. 26SD172, A) Tel. Rec. 167-14
5267, 5268 (Ch. 26SD172, A) Tel. Rec. 167-14
5270 (Ch. 26SD172C) Tel. Rec. 167-14
5271 (Ch. 26SD172C) Tel. Rec. (See Model 5207—Set 167-14) 5272, 5273 (Ch. 26SD172C) Tel. Rec. 167-14
5280, 5281 (Ch. 215212) Tel. Rec. 201-10
5288, 5289 (Ch. 25CD202) Tel. Rec. 178-11
5290 (Ch. 25SD202) Tel. Rec. 178-11
5291, 5292, 5293, 5294, 5295 (Ch. 25CD202) Tel. Rec. 178-11
5296A, 5297A (Ch. 25CD202) Tel. Rec. 178-11
5296, 5297 (Ch. 25SD202) Tel. Rec. 178-11
5298 (Ch. 25CD202) Tel. Rec. 178-11
5299 (Ch. 25CD202) Tel. Rec. (See Model 5298—Set 178-11) 5301 (Ch. 215173-D) Tel. Rec. 201-10
5325 (Ch. 25D173A) Tel. Rec. 222-14
5325A (Ch. 27D173) Tel. Rec. 222-14
5326 (Ch. 25D173A) Tel. Rec. 222-14
5326A (Ch. 27D173) Tel. Rec. 222-14
5340, 5341 (Ch. 215213) Tel. Rec. 201-10
5342 (Ch. 25D213) Tel. Rec. (See PCB 104—Set 250-1 and Model 5342A—Set 210-11) 5342A (Ch. 27D213) Tel. Rec. 210-11
5343 (Ch. 25D213) Tel. Rec. (See PCB 104—Set 250-1 and Model 5342A—Set 210-11) 5343A (Ch. 27D213) Tel. Rec. 210-11

SPARTON—Cont.

5362 (Ch. 25D173A) Tel. Rec. 222-14
5362A (Ch. 27D173) Tel. Rec. 222-14
5363 (Ch. 25D173A) Tel. Rec. 222-14
5363A (Ch. 27D173) Tel. Rec. 222-14
5380, 5381 (Ch. 215213) Tel. Rec. 201-10
5382 (Ch. 25D213) Tel. Rec. (See PCB 104—Set 250-1 and Model 5342A—Set 210-11) 5382A (Ch. 27D213) Tel. Rec. 210-11
5382B (Ch. 27D213-A) Tel. Rec. 210-11
5383 (Ch. 25D213) Tel. Rec. (See PCB 104—Set 250-1 and Model 5342A—Set 210-11) 5383A (Ch. 27D213) Tel. Rec. 210-11
5383B (Ch. 27D213A) Tel. Rec. (See Model 5382B—Set 210-11) 5384 (Ch. 25D213) Tel. Rec. (See PCB 104—Set 250-1 and Model 5342A—Set 210-11) 5384A (Ch. 27D213) Tel. Rec. 210-11
5385 (Ch. 25D213) Tel. Rec. (See PCB 104—Set 250-1 and Model 5342A—Set 210-11) 5386 (Ch. 25D213) Tel. Rec. (See PCB 104—Set 250-1 and Model 5342A—Set 210-11) 5386A (Ch. 27D213) Tel. Rec. 210-11
5386B (Ch. 27D213A) Tel. Rec. (See Model 5382B—Set 210-11) 5387B (Ch. 27D213A) Tel. Rec. (See Model 5382B—Set 210-11) 5390 (Ch. 25D213) Tel. Rec. (See PCB 104—Set 250-1 and Model 5342A—Set 210-11) 5391 (Ch. 25D213) Tel. Rec. (See PCB 104—Set 250-1 and Model 5342A—Set 210-11) 10352 (Ch. 27D213 and Radio Ch. 8W10) Tel. Rec. (For TV Ch. see Set 210-11; for Radio Ch. see Model 141XX—Set 126-12) 10352A (Ch. 27D213A and Radio Ch. 8W10) Tel. Rec. (For TV Ch. see Model 5382B—Set 210-11; for Radio Ch. see Model 141XX—Set 126-12) 10353 (Ch. 27D213 and Radio Ch. 8W10) Tel. Rec. (For TV Ch. see Set 210-11; for Radio Ch. see Model 141XX—Set 126-12) 10353A (Ch. 27D213A and Radio Ch. 8W10) Tel. Rec. (For TV Ch. see Model 5382B—Set 210-11; for Radio Ch. see Model 141XX—Set 126-12) 11322, 11324 (Ch. 215213A) Tel. Rec. (See Model 5240—Set 201-10) 11342 (Ch. 27D213A and Radio Ch. 8W10) Tel. Rec. (For TV Ch. see Model 5382B—Set 210-11; for Radio Ch. see Model 141XX—Set 126-12) 15312, 15314 (Ch. 215213A) Tel. Rec. (See Model 5240—Set 201-10) 22312, 22313 (Ch. 29U213) Tel. Rec. 232-8
23322, 23323 (Ch. 29U213) Tel. Rec. 232-8
24542 (Ch. 29U273) Tel. Rec. 224-13
25544 (Ch. 29U273) Tel. Rec. 224-13
26542 (Ch. 27D273) Tel. Rec. 224-13
26544 (Ch. 27D273) Tel. Rec. 224-13
Ch. PC-5-26 (See Model 6AW26-PA)
Ch. 2RD190 (See Model 5085)
Ch. 25SD201 (See Model 5170)
Ch. 310 (See Model 6944)
Ch. 3T110 (See Model 4916)
3AR1 217-17
Ch. 3TR10 (See Model 5052)
Ch. 3TV9, 3TV9C (See Model 4900-TV)
Ch. 4E3 (See Model 301)
Ch. 4E10 (See Model 150)
Ch. 5A7 (See Model 100)
Ch. 5-06 (See Model 3AW06)
Ch. 5A10 (See Model 130)
Ch. 5B3C (See Model 320C)
Ch. 5C3 (See Model 342)
Ch. 5-16 (See Model 5A116)
Ch. 5-26PS (See Model 5AW26PS)
Ch. 669 (See Model 1051)
Ch. 613 (See Model 350)
Ch. 618 (See Model 1030)
Ch. 6-06 (See Model 6AM06)
Ch. 717 (See Model 1010)
Ch. 7-46 (See Model 7AM46)
Ch. 819 (See Model 121)
Ch. 819A (See Model 141A)
Ch. 8510 (See Model 4970)
Ch. 8W10 (See Model 141XX)
Ch. 8-46 (See Model 8AM46)
Ch. 8-57 (See Model 1005)
Ch. 918 (See Model 1035)
Ch. 918A (See Model 4900TV)
Ch. 10-77PA (See Model 10BW76PA)
Ch. 1217 (See Model 1000)
Ch. 19TS10, 19TS10A (See Model 5010)
Ch. 215172 (See Model 5212)
Ch. 215173-D (See Model 5301)
Ch. 215212 (See Model 5240)
Ch. 215213 (See Model 5340)
Ch. 21513A (See Model 11322)
Ch. 23T810 (See Model 4964)
Ch. 23TC10 (See Model 4935)
Ch. 23TD10 (See Model 5002)
Ch. 24TR10 (See Model 4944)
Ch. 24T10 (See Model 4916)
Ch. 24T10 (See Model 4920)
Ch. 24T10 (See Model 4935)
Ch. 24T10 (See Model 4944)
Ch. 24T10 (See Model 4954)
Ch. 24T10 (See Model 4964)
Ch. 24T10 (See Model 4970)
Ch. 24T10 (See Model 4980)
Ch. 24T10 (See Model 4990)
Ch. 24T10 (See Model 5000)
Ch. 24T10 (See Model 5010)
Ch. 24T10 (See Model 5020)
Ch. 24T10 (See Model 5030)
Ch. 24T10 (See Model 5040)
Ch. 24T10 (See Model 5050)
Ch. 24T10 (See Model 5060)
Ch. 24T10 (See Model 5070)
Ch. 24T10 (See Model 5080)
Ch. 24T10 (See Model 5090)
Ch. 24T10 (See Model 5100)
Ch. 24T10 (See Model 5110)
Ch. 24T10 (See Model 5120)
Ch. 24T10 (See Model 5130)
Ch

SYLVANIA—Cont.

320 Series (Ch. 1-520-1, -3) Tel. Rec. (Also See PCB 100—Set 245-1) 234-13
 320 "U" Series (Ch. 1-520-4) Tel. Rec. (Also See PCB 100—Set 245-1) 234-13
 321 Series (Ch. 1-520-5) Tel. Rec. (See PCB 100—Set 245-1 and Model 120-20 Series—Set 234-13) 234-13
 321 "U" Series (Ch. 1-520-6) Tel. Rec. (See PCB 100—Set 245-1 and Model 120-20 "U" Series—Set 234-13) 234-13
 321-1 Series (Ch. 1-520-0, -7) Tel. Rec. (See PCB 100—Set 245-1 and Model 326 Series—Set 234-13) 234-13
 325 Series (Ch. 1-520-1, -3) Tel. Rec. (Also See PCB 100—Set 245-1) 234-13
 325 "U" Series (Ch. 1-520-4) Tel. Rec. (Also See PCB 100—Set 245-1) 234-13
 326 Series (Ch. 1-520-0, -7) Tel. Rec. (Also See PCB 100—Set 245-1) 234-13
 326 "U" Series (Ch. 1-520-8) Tel. Rec. (Also See PCB 100—Set 245-1) 234-13
 331 Series (Ch. 1-513-1, -3) Tel. Rec. (Also See PCB 17—Set 189-1) 248-9
 331 "U" Series (Ch. 1-513-2, -4) Tel. Rec. (Also See PCB 17—Set 189-1) 248-9
 336 Series (Ch. 1-513-1, -3) Tel. Rec. (Also See PCB 17—Set 189-1) 248-9
 336 "U" Series (Ch. 1-513-2, -4) Tel. Rec. (Also See PCB 17—Set 189-1) 248-9
 372 Series (Ch. 1-518-1, -3) Tel. Rec. (See Model 175-18—Set 229-15) 229-15
 372 "U" Series (Ch. 1-518-2) Tel. Rec. (See Model 175-18—Set 229-15) 229-15
 372 "U" Series (Ch. 1-518-6) Tel. Rec. (See Model 175-18—Set 229-15) 229-15
 373 Series (Ch. 1-518-1, -3 and Radio Ch. 1-603-1) Tel. Rec. (For TV Ch. See Set 229-15, For Radio Ch. See Model 178B—Set 192-9) 229-15
 373 Series (Ch. 1-518-5 and Radio Ch. 1-603-1) Tel. Rec. (For TV Ch. See Set 229-15, For Radio Ch. See Model 178B—Set 192-9) 229-15
 373 "U" Series (Ch. 1-518-2, -4 and Radio Ch. 1-603-1) Tel. Rec. (For TV Ch. See Set 229-15, For Radio Ch. See Model 178B—Set 192-9) 229-15
 373 "U" Series (Ch. 1-518-6) and Radio Ch. 1-603-1) Tel. Rec. (For TV Ch. See Set 229-15, For Radio Ch. See Model 178B—Set 192-9) 229-15
 375 Series (Ch. 1-518-1, -3) Tel. Rec. (See Model 175-18—Set 229-15) 229-15
 375 "U" Series (Ch. 1-518-2) Tel. Rec. (See Model 175-18—Set 229-15) 229-15
 375 "U" Series (Ch. 1-518-6) Tel. Rec. (See Model 175-18—Set 229-15) 229-15
 376 Series (Ch. 1-518-1, -3) Tel. Rec. (See Model 175-18—Set 229-15) 229-15
 376 "U" Series (Ch. 1-518-2) Tel. Rec. (See Model 175-18—Set 229-15) 229-15
 376 "U" Series (Ch. 1-518-6) Tel. Rec. (See Model 175-18—Set 229-15) 229-15
 377 Series (Ch. 1-518-1, -3) Tel. Rec. (See Model 175-18—Set 229-15) 229-15
 377 "U" Series (Ch. 1-518-2) Tel. Rec. (See Model 175-18—Set 229-15) 229-15
 377 "U" Series (Ch. 1-518-6) Tel. Rec. (See Model 175-18—Set 229-15) 229-15
 386B (Ch. 1-512-1) Tel. Rec. 220-10
 386BU (Ch. 1-512-2) Tel. Rec. 220-10
 386M (Ch. 1-512-1) Tel. Rec. 220-10
 386MU (Ch. 1-512-2) Tel. Rec. 220-10
 401 Series (Ch. 1-514-5) Tel. Rec. (See PCB 100—Set 245-1 and Model 301 Series—Set 234-13) 234-13
 401 "U" Series (Ch. 1-514-6) Tel. Rec. (See PCB 100—Set 245-1 and Model 301 "U" Series—Set 234-13) 234-13
 410 Series (Ch. 1-530-1) Tel. Rec. (See PCB 100—Set 245-1 and Model 105-14 Series—Set 234-13) 234-13
 410 "U" Series (Ch. 1-530-2) Tel. Rec. (See PCB 100—Set 245-1 and Model 105-14 "U" Series—Set 234-13) 234-13
 420 Series (Ch. 1-520-1, -3) Tel. Rec. (See PCB 100—Set 245-1 and Model 320 Series—Set 234-13) 234-13
 420 "U" Series (Ch. 1-520-4) Tel. Rec. (See PCB 100—Set 245-1 and Model 320 "U" Series—Set 234-13) 234-13
 421 "U" Series (Ch. 1-520-6) Tel. Rec. (See PCB 100—Set 245-1 and Model 120-20 "U" Series—Set 234-13) 234-13
 425 "U" Series (Ch. 1-520-6) Tel. Rec. (See PCB 100—Set 245-1 and Model 120-20 "U" Series—Set 234-13) 234-13
 430L (Ch. 1-254) 165-15
 433B, GR, H, LU, RE, YE (Ch. 1-604-1) 225-17

SYLVANIA—Cont.

454BR, GR, H, RE (Ch. 1-606-1) 247-12
 510B, 510H, 510W (Ch. 1-215) 103-16
 511B, H, M, 512BR, CH, GR, RE, YE (Ch. 1-601-1) 160-12
 512B, CH, GR, H, M, RE, YE (Ch. 1-601-2) 221-11
 540B, BA, 540H, HA, 540M, MA 119-11
 541B, H, M, 542BR, CH, GR, RE, YE (Ch. 1-602-1) 159-13
 543 (Ch. 1-602-2) 225-18
 563B (Ch. 1-602-3) 221-11
 593 (Ch. 1-602-3) 225-18
 1110X (Ch. 1-329) Tel. Rec. (See PCB 47—Set 181-1 and Model 1210X—Set 128-16) 128-16
 1210X (Ch. 1-31) Tel. Rec. (Also See PCB 44—Set 178-1) 128-16
 2108M, M, W (Ch. 1-462) Tel. Rec. (See PCB 55—Set 189-1 and Model 5130B—Set 120-10) 124-10
 2140B, M (Ch. 1-462) Tel. Rec. (See PCB 55—Set 189-1 and Model 5140B—Set 120-10) 124-10
 2221M (Ch. 1-387) Tel. Rec. 137-13
 4120M (Ch. 1-260) Tel. Rec. (Also See PCB 55—Set 189-1) 124-10
 4130B, E, M, W (Ch. 1-260) Tel. Rec. (Also See PCB 55—Set 189-1) 124-10
 5130B, M, W (Ch. 1-290) Tel. Rec. (Also See PCB 17—Set 128-1) 120-10
 5140B, M (Ch. 1-290) Tel. Rec. (Also See PCB 17—Set 128-1) 120-10
 5150M (Ch. 1-274) Tel. Rec. 131-15
 6110X (Ch. 1-261) Tel. Rec. (Also See PCB 55—Set 189-1) 124-10
 6120B, M, W (Ch. 1-261) Tel. Rec. (Also See PCB 55—Set 189-1) 124-10
 7110X (Ch. 1-366) Tel. Rec. (Also See PCB 55—Set 189-1) 124-10
 7110XB (Ch. 1-441) Tel. Rec. (See PCB 55—Set 189-1 and Model 7110X—Set 124-10) 124-10
 7110XF (Ch. 1-366-66) Tel. Rec. (Also See PCB 55—Set 189-1) 124-10
 7110XFA (Ch. 1-442) Tel. Rec. 131-15
 7111M (Ch. 1-441) Tel. Rec. (See PCB 55—Set 189-1 and Model 7110X—Set 124-10) 124-10
 7111MA (Ch. 1-366) Tel. Rec. (See PCB 55—Set 189-1 and Model 7110X—Set 124-10) 124-10
 7120 (Ch. 1-366) Tel. Rec. (Also See PCB 55—Set 189-1) 124-10
 7120BF (Ch. 1-366-66) Tel. Rec. (Also See PCB 55—Set 189-1) 124-10
 7120M (Ch. 1-366) Tel. Rec. (Also See PCB 55—Set 189-1) 124-10
 7120MF (Ch. 1-366-66) Tel. Rec. (Also See PCB 55—Set 189-1) 124-10
 7120MFA (Ch. 1-442) Tel. Rec. 131-15
 7120W (Ch. 1-366) Tel. Rec. (Also See PCB 55—Set 189-1) 124-10
 7120WF (Ch. 1-366-66) Tel. Rec. (Also See PCB 55—Set 189-1) 124-10
 7130B (Ch. 1-366) Tel. Rec. (Also See PCB 55—Set 189-1) 124-10
 7130BF (Ch. 1-366-66) Tel. Rec. (Also See PCB 55—Set 189-1) 124-10
 7130E, M (Ch. 1-366) Tel. Rec. (Also See PCB 55—Set 189-1) 124-10
 7130MF (Ch. 1-366-66) Tel. Rec. (Also See PCB 55—Set 189-1) 124-10
 7130MFA (Ch. 1-442) Tel. Rec. 131-15
 7130W (Ch. 1-366) Tel. Rec. (Also See PCB 55—Set 189-1) 124-10
 7130WF (Ch. 1-366-66) Tel. Rec. (Also See PCB 55—Set 189-1) 124-10
 7140M, W (Ch. 1-356) Tel. Rec. (See PCB 55—Set 189-1 and Model 6140M—Set 120-10) 124-10
 7140MA, 7140WA (Ch. 1-437) Tel. Rec. 131-15
 7150M (Ch. 1-357) Tel. Rec. 131-15
 7160B (Ch. 1-357) Tel. Rec. 131-15
 Ch. 1-108 (See Model 122M-1) 124-10
 Ch. 1-139 (See Model 1-075) 124-10
 Ch. 1-168 (See Model 1-090) 124-10
 Ch. 1-186 (See Model 1-125-1) 124-10
 Ch. 1-215 (See Model 1-250) 124-10
 Ch. 1-260 (See Model 4120M) 124-10
 Ch. 1-261 (See Model 6110X) 124-10
 Ch. 1-271 (See Model 6140M) 124-10
 Ch. 1-274 (See Model 5150M) 124-10
 Ch. 1-290 (See Model 5130B) 124-10
 Ch. 1-356 (See Model 748) 124-10
 Ch. 1-357 (See Model 7150M) 124-10
 Ch. 1-366 (See Model 7110X) 124-10
 Ch. 1-366-66 (See Model 7110XF) 124-10
 Ch. 1-381 (See Model 1210X) 124-10
 Ch. 1-387 (See Model 2221M) 124-10
 Ch. 1-387-1 (See Model 222M-1) 124-10
 Ch. 1-437 (See Model 7140MA) 124-10
 Ch. 1-437-1 (See Model 748-1) 124-10
 Ch. 1-437-2 (See Model 748-2) 124-10
 Ch. 1-437-3 (See Model 738-5) 124-10
 Ch. 1-437-3 (Codes CO6 and up) (See Model 150A) 124-10
 Ch. 1-441 (See Model 7110XB) 124-10
 Ch. 1-442 (See Model 7110XFA) 124-10
 Ch. 1-462-1 (See Model 24M) 124-10
 Ch. 1-502-1 (See Model 71M-1) 124-10

SYLVANIA—Cont.

Ch. 1-502-2 (See Model 73M-1) 124-10
 Ch. 1-502-3 (See Model 73M-1) 124-10
 Ch. 1-504-1 (See Model 105B) 124-10
 Ch. 1-504-2, -4 (See Model 105BU) 124-10
 Ch. 1-507-1 (See Model 228-11) 124-10
 Ch. 1-508-1 (See Model 172K) 124-10
 Ch. 1-508-2 (See Model 172KU) 124-10
 Ch. 1-510-1 (See Model 120B) 124-10
 Ch. 1-510-2, -4 (See Model 120BU) 124-10
 Ch. 1-512-1 (See Model 386B) 124-10
 Ch. 1-512-2 (See Model 386BU) 124-10
 Ch. 1-513-1 (See Model 331 Series) 124-10
 Ch. 1-513-2 (See Model 331 "U" Series) 124-10
 Ch. 1-513-3 (See Model 331 Series) 124-10
 Ch. 1-513-4 (See Model 331 "U" Series) 124-10
 Ch. 1-514-1, -3 (See Model 105-14 Series) 124-10
 Ch. 1-514-4 (See Model 105-14 "U" Series) 124-10
 Ch. 1-514-5 (See Model 301 Series) 124-10
 Ch. 1-514-6 (See Model 301 "U" Series) 124-10
 Ch. 1-518-1 (See Model 175-18 Series) 124-10
 Ch. 1-518-2 (See Model 175-18 "U" Series) 124-10
 Ch. 1-518-3 (See Model 175-18 Series) 124-10
 Ch. 1-518-5 (See Model 372 Series) 124-10
 Ch. 1-518-6 (See Model 372 "U" Series) 124-10
 Ch. 1-520-0 (See Model 326 Series) 124-10
 Ch. 1-520-1, -3 (See Model 120-20 Series) 124-10
 Ch. 1-520-4 (See Model 120-20 "U" Series) 124-10
 Ch. 1-520-5 (See Model 321 Series) 124-10
 Ch. 1-520-6 (See Model 321 "U" Series) 124-10
 Ch. 1-520-7 (See Model 326 Series) 124-10
 Ch. 1-520-8 (See Model 326 "U" Series) 124-10
 Ch. 1-530-1 (See Model 410 Series) 124-10
 Ch. 1-601-1 (See Model 511B) 124-10
 Ch. 1-601-2 (See Model 513B) 124-10
 Ch. 1-601-3 (See Model 503B) 124-10
 Ch. 1-602-1 (See Model 541B) 124-10
 Ch. 1-602-2 (See Model 543) 124-10
 Ch. 1-602-3 (See Model 593) 124-10
 Ch. 1-603-1 (See Model 178B) 124-10
 Ch. 1-604-1 (See Model 433B) 124-10
 Ch. 1-606-1 (See Model 454BR) 124-10

SYLVANIA—Cont.

512 Tel. Rec. 88-12
 516 Tel. Rec. (See Model 114—Set 141-13) 88-12
 612 Tel. Rec. 88-12
 710 Tel. Rec. 88-12
 712 Tel. Rec. (See Model 410—Set 88-12) 129-12
 816-3CR Tel. Rec. (For TV Ch. only see Model 162—Set 129-12) 129-12
 916C Tel. Rec. 129-12
 916CAF Tel. Rec. (For TV Ch. only see Model 162—Set 129-12) 129-12
 9192C Tel. Rec. 141-13
 919CAF Tel. Rec. (For TV Ch. only see Model 114—Set 141-13) 141-13
 920 (Ch. TVG) Tel. Rec. (See Model 201—Set 131-16) 101-13
 1014 (Ch. TVG) Tel. Rec. (See Model 201—Set 131-16) 101-13
 1016 (Ch. TVG) Tel. Rec. (See Model 201—Set 131-16) 101-13
 Ch. RD-1 (See Model RK41) 101-13
 Ch. TVG Tel. Rec. (See Model 201) Ch. TVJ (See Model K21) 101-13

TELE-KING—Cont.

1635 20-22
 1642 20-23
 1643 21-34

TELEQUIP

5135, 5136, 5140A, 11-24

TELESONIC (Medco)

1635 20-22
 1642 20-23
 1643 21-34

TELE-TONE

TV149 Tel. Rec. 56-22
 TV170 Tel. Rec. 83-12
 TV208 Tel. Rec. 90-11
 TV208TR Tel. Rec. 95-6
 TV209 Tel. Rec. (See PCB 21—Set 136-1 and Model TV-249—Set 57-21) 95-6
 TV-220 Tel. Rec. (Also see PCB 21—Set 136-1) 57-21
 TV-230 Tel. Rec. 91-13
 TV-240 Tel. Rec. 91-13
 TV-255 Tel. Rec. (Ch. TS) Tel. Rec. 101-13
 TV-259 Tel. Rec. (See Model TV-249—Set 57-21) 101-13
 TV-282 Tel. Rec. 71-14
 TV-283 Tel. Rec. (See Model TV-285—Set 87-13) 93-10
 TV-284 Tel. Rec. 87-13
 TV-285, 287, 288 Tel. Rec. 93-10
 TV-300, TV-301 (Ch. TAA, TAB) Ch. TAA, TV-301 (Ch. TW) Tel. Rec. 107-10
 TV-304, TV-305 (Ch. TAA, TAB) Tel. Rec. 99A-12
 TV-304, TV-305 (Ch. TX) Tel. Rec. 107-10
 TV-306, TV-307 (Ch. TV, TZ) Tel. Rec. 104-12
 TV-308 (Ch. TAC) Tel. Rec. 109-14
 TV-314 (Ch. TAJ) Tel. Rec. 125-12
 TV-315 (Ch. TAA, TAB) Tel. Rec. 115-13
 TV-316 (Ch. TAH) Tel. Rec. 125-13
 TV-318 (Ch. TAM) Tel. Rec. 124-11
 TV-322, TV-323 (Ch. TAM) Tel. Rec. 124-11
 TV-324, TV-325, TV-326 (Ch. TAP, TAP-1, TAP-2) Tel. Rec. 127-12
 TV-328, TV-329 (Ch. TAP, TAP-1, TAP-2) Tel. Rec. 127-12
 TV-330, TV-331, TV-332, TV-333 (Ch. TAO) Tel. Rec. 145-11
 TV-335, TV-336 (Ch. TAP, TAP-1, TAP-2) Tel. Rec. 127-12
 TV-340 (Ch. TAP, TAP-1, TAP-2) Tel. Rec. 127-12
 TV-345 (Ch. TAP, TAP-1, TAP-2) Tel. Rec. 127-12
 TV-348, TV-349 (Ch. TAP-2) Tel. Rec. (See Model TV-324—Set 127-12) 127-12
 TV-352 Tel. Rec. (See Model TV-324—Set 127-12) 127-12
 TV-355 (Ch. 8001, 8002, 8003) Tel. Rec. 145-11
 TV-357 (Ch. 8001, 8002, 8003) Tel. Rec. 145-11
 TV-358, TV-359 (See Model TV-324—Set 127-12) 127-12
 TV-360, TV-365 (Ch. 8001, 8002, 8003) Tel. Rec. 145-11
 TV-374 (Ch. 8001, 8002, 8003) Tel. Rec. (See PCB 35—Set 164-11 and Model TV-330—Set 145-11) 145-11
 TV-385-U, TV-386-U (Ch. 8013, 8015) Tel. Rec. 27-27
 100, 100-A, 101, 109 (Ch. Series G-723) 24-27
 109 (Ch. Series N) 8-30
 110 (See Model 117-A—Set 1-35) 11-13
 111, 113 39-26
 117-A (Ch. Series "D") 1-35
 119, 120 (See Model 117-A—Set 1-35) 1-35
 122, 123 39-26
 124 (See Model 117-A—Set 1-35) 39-26
 125 39-26
 126 (See Model 117-A—Set 1-35) 39-26
 127, 130, 131 39-26
 132 (See Model 117-A—Set 1-35) 11-25
 133 13-32
 134 13-32
 135 14-29
 138 (Ch. Series N) 23-27
 139, 140, 141 (Ch. Series "H") (See Model 135—Set 142-9) 23-27
 142, 143, 144 (See Model 145—Set 23-28) 23-28
 145 (Ch. Series "R") 23-28
 148 (Ch. Series "S") 24-26
 149 (Ch. Series "H") (See Model 135—Set 142-9) 38-25
 150 (Ch. Series "T") 38-25
 151 (Ch. Series "S") (See Model 148—Set 24-26) 76-18

TELE-TONE—Cont.

152 (Ch. Series "R") (See Model 145—Set 23-28) 35-23
 156 (Ch. Series U) 35-23
 157 (Ch. Series "H") (See Model 135—Set 142-9) 49-24
 157 (Ch. Series AE) 49-24
 158 (Ch. Series AT) 59-20
 159 (Ch. Series AA) 38-26
 160 (Ch. Series Y) 36-24
 161, 162 (Ch. Series T) 38-25
 163, 164 (Ch. Series "H") (See Model 135—Set 142-9) 50-20
 165 (Ch. Series AG) 50-20
 166 (Ch. Series AE) 49-24
 167, 168, 171 (Ch. Series T) 38-25
 172 (Ch. Series U) 35-23
 174 (Ch. Series U) 38-25
 176 (Ch. Series U) 35-23
 182 51-22
 183 53-24
 185 (Ch. Series AH) 52-21
 190 (Ch. Series AZ) 61-19
 195 (Ch. Series BH) 71-15
 198 59-20
 200 (Ch. Series "AZ") (See Model 190—Set 61-19) 74-9
 201 (Ch. Series AX) 74-9
 205 (Ch. Series BD) 73-12
 206 127-11
 214 (Ch. Series "AZ") (See Model 190—Set 61-19) 144-13
 215 (Ch. Series BD) (See Model 205—Set 73-12) 144-13
 228 (Ch. BL) 144-13
 232 (Ch. Series "BP") (See Model 205—Set 73-12) 141-14
 235 (Ch. BO) 141-14
 Ch. Series A (See Model 100) 90-11
 Ch. Series AE (See Model 159) 95-6
 Ch. Series AG (See Model 157) 95-6
 Ch. Series AH (See Model 165) 95-6
 Ch. Series AI (See Model 185) 95-6
 Ch. Series AJ (See Model 158) 95-6
 Ch. Series AK (See Model 201) 95-6
 Ch. Series AL (See Model 196) 95-6
 Ch. Series AM (See Model 205) 95-6
 Ch. Series AN (See Model 195) 95-6
 Ch. Series AO (See Model 228) 95-6
 Ch. Series AP (See Model 134) 95-6
 Ch. Series AQ (See Model 137A) 95-6
 Ch. Series AR (See Model 135) 95-6
 Ch. Series AS (See Model 109) 95-6
 Ch. Series AT (See Model 138) 95-6
 Ch. Series AU (See Model 145) 95-6
 Ch. Series AV (See Model 148) 95-6
 Ch. Series T (See Model 150) 95-6
 Ch. TAA, TAB (See Model TV-315) 95-6
 Ch. TAC (See Model TV-308) 95-6
 Ch. TAH (See Model TV-316) 95-6
 Ch. TAJ (See Model TV-314) 95-6
 Ch. TAM (See Model TV-318) 95-6
 Ch. TAO (See Model TV-330) 95-6
 Ch. TAP, TAP-1, TAP-2 (See Model TV-324) 95-6
 Ch. TS (See Model TV-255) 95-6
 Ch. TW, TX (See Model TV-300) 95-6
 Ch. TZ (See Model TV-306) 95-6
 Ch. Series Y (See Model 160) 95-6
 Ch. 8001, 8002, 8003 (See Model TV-355) 95-6
 Ch. 8013 (See Model TV-385-U) 95-6
 Ch. 8015 (See Model TV-386-U) 95-6

TELE-VOGUE (See Muntz)

TELEVOX

27B-2W 22-29
 27K-W 20-33
 27P-T 22-28

TEL-VAR (See Audar)

TEMPLE

E-301 21-35
 E-510 2-3
 E-511 11-26
 E-512, E-514 (See Model E-510—Set 2-3) 2-3
 E-519 2-3
 F-101 12-26
 F-611 9-32
 F-616 5-38
 F-617 12-27
 G-410 27-28
 G-415 43-18
 G-416 G-419 25-25
 G-513 23-29
 G-515 17-34
 G-516 18-31
 G-518 29-27
 G-521 28-33
 G-522 26-26
 G-619 22-30
 G-622 44-24
 G-721 (See Model G-722—Set 24-27) 24-27
 G-722 24-27
 G-723 (See Model G-722—Set 24-27) 24-27
 G-724 38-27
 G-725 34-23
 G-1430 43-19
 G-1435 (See Model G-418—Set 26-25) 26-25
 G-7205 (See Model G-722—Set 24-27) 24-27
 H-411 47-23
 H-521 (See Model G-521—Set 28-33) 28-33
 H-622 44-24
 H-727 (See Model G-725—Set 34-23) 34-23
 TV-1776, TV-1777, TV-1778, TV-1779 Tel. Rec. 66-16

TEMPOTONE

500 E Series 2-8

TEMPLETON (See Temple)

THORDARSON

THORENS—WESTINGHOUSE

THORENS (See Record Changer Listing)

TRAD

C-2020, C-2420, CD2020 Tel. Rec. 173-14

T-20, A Tel. Rec. 133-14

T-20-E, A Tel. Rec. 167-17A

T-1720 Tel. Rec. 173-14

T-1853, A Tel. Rec. 200-10

TRANSIVISION

Ch. Model A Tel. Rec. 107-11

Ch. A-3 Tel. Rec. 130-15

Ch. A-4 Tel. Rec. 192-10

WRS-3 Tel. Rec. 112-10

TRANSVue

17XC, 17XT Tel. Rec. (Similar to Chassis) 132-8

20XC, 20XT Tel. Rec. (Similar to Chassis) 132-8

601 (Ch. 16AX23, 25, 26) Tel. Rec. (Similar to Chassis) 99-14

61 (Ch. 16AX23, 25, 26) Tel. Rec. (Similar to Chassis) 99-14

1400T Tel. Rec. (Similar to Chassis) 132-8

1700C, T Tel. Rec. (Similar to Chassis) 132-8

2000C Tel. Rec. (Similar to Chassis) 132-8

TRAV-LER (Also see Record Changer Listing)

10T Tel. Rec. 86-11

12L50, A Tel. Rec. 108-13

12T Tel. Rec. 86-11

14B50, A, 14C50, A Tel. Rec. 108-13

16G50A Tel. Rec. 108-13

16R50A, 16T50A Tel. Rec. 108-13

16T Tel. Rec. (Also see PCB 31) 108-13

20A50 Tel. Rec. 146-11

62R50, 63R50 Tel. Rec. 150-13

64R50, 64R50-1, 64R50-2 Tel. Rec. 146-11

65G50, -1, -2 Tel. Rec. (See Model 20A50—Set 146-11)

75A50, 75A50-1, 75A50-2 Tel. Rec. 146-11

114-A, -2 (Ch. 32A1) Tel. Rec. 150-13

117-3, -4, -6 (Ch. 32A1) Tel. Rec. 150-13

119-5 (Ch. 32A1) Tel. Rec. 150-13

217, -10, -11, -12, -14 (Ch. 32A2) Tel. Rec. 171-11

217-15, 217-16 (Ch. 34A2) Tel. Rec. 170-14

217-25 (Ch. 34A2) Tel. Rec. (See Model 217-15—Set 170-14)

217-27 (Ch. 35B2) Tel. Rec. (See Model 217-15—Set 170-14)

219-8A, 219-8B (Ch. 11A2) Tel. Rec. 162-14

220-9, -9A, -9B (Ch. 33A2) Tel. Rec. 171-11

220-22, -23, -24, -27 (Ch. 34A2) Tel. Rec. (See Model 217-15—Set 170-14)

317-44, A (Ch. 46B3) Tel. Rec. 240-10

317-47 (Ch. 46A3) Tel. Rec. 240-10

321-46, 321-48 (Ch. 46A3) Tel. Rec. 240-10

5000 (See Model 5000—Set 11-27)

50001 11-27

5002 Series (Ch. 109) 12-28

5007, 5008, 5009 (Ch. 104) 1-36

5010, 5011, 5012 (Ch. 105) 2-5

5015 36-25

5019 23-30

5020 (Ch. 800) 1-28

5021 43-20

5022 101-14

5027 31-30

5028 34-24

5030, 5031 33-29

5036 54-19

5049 45-24

5051 32-26

5054 36-26

5056-A 90-12

5060, 5061 116-11

5066 42-24

5100 163-13

5170 223-13

5301 224-15

5372 243-12

5376 246-10

6040 49-20

6050 56-23

6053 (See Model 6050—Set 56-23)

7000, 7001 59-21

7003 (Ch. 501) 12-29

7014 59-21

7016, 7017 84-11

7023 83-13

7036 112-11

Ch. 11A2 (See Model 219-8A)

Ch. 32A1 (See Model 62R50)

Ch. 33A2 (See Model 217-15)

Ch. 34A2 (See Model 217-15)

Ch. 35B2 (See Model 217-27)

Ch. 46A3 (See Model 317-47)

Ch. 46B3 (See Model 317-44)

Ch. 104 (See Model 5007)

Ch. 105 (See Model 5010)

Ch. 109 (See Model 5002)

Ch. 501 (See Model 7003)

Ch. 800 (See Model 5021)

TRELA

HW301 14-28

TRUETONE

D1034A, B, C (See Model D1046A—Set 102-15)

D1046A 102-15

D1046B, C, D (See Model D1046A—Set 102-15)

D1092 Tel. Rec. (Similar to Chassis) 108-7

TRUETONE—Cont.

D-1234A, B 189-15

D1240A 187-12

D1435A, D1436A 239-10

D1612 28-34

D1644 12-30

D1645 (Factory 26A76-650) 6-33

D1748 37-27

D1752 (Factory 7901-14) 34-25

D1835 (Factory Model 25A86-856) 44-25

D1836, D1836A (Factory 26A85-856) 45-25

D1840 (Fact. No. 138PCXM) 41-24

D1845A, B, C 40-23

D1850 (Series A) 51-23

D1949 60-20

D1950, D1951 (See Model D1850—Set 51-23)

D1952 (See Model D1949—Set 60-20)

D1990 (Factory No. 74F22) Tel. Rec. 69-13

D1991, B Tel. Rec. 77-11

D1992 (Factory No. 74F22) Tel. Rec. 69-13

D1993, B Tel. Rec. 77-11

D1994 Tel. Rec. 77-11

D1996 Tel. Rec. (See Model D2983—Set 68-18)

D2017, D2018 101-15

D2020 106-15

D2025A (Fact. Mod. 26A95-906) 83-14

D2027A 97-18

D2102A, B 200-11

D2103A, B 200-11

D2108A, D2109A 197-13

D2145 197-14

D2205 201-12

D2214A 204-10

D2226 196-16

D2237A 182-15

D2255 197-14

D2261 190-14

D2270 211-16

D2325-A 205-11

D2383 199-15

D2386, D2387, D2388 230-13

D2389 231-16

D2410A, D2411A, D2412A, D2413A 225-19

D2603 (Factory Model 4611) 13-33

D2604 13-34

D2605 (Factory Model 2AW2) 9-34

D2606 65-15

D2612 (Code SW-9022-G) 3-9

D2613 13-37

D2615 (Factory Model 6D110) 2-18

D2616 (Factory Model 6D117) 10-32

D2616-B 31-32

D2619 (Factory No. 2701) 27-19

D2620 1-28

D2621 4-32

D2622 14-30

D2623 11-29

D2624 (Factory 27D14-600) 2-18

D2626 (Fact. No. 457-2) 52-22

D2630 (Factory 27D14-602 Issue A) 1-10

D2634 12-31

D2640 (Factory No. 459) 43-21

D2642 12-32

D2645 (Factory No. 101C) 11-30

D2645 4-39

D2661 (Factory 4B19) 2-23

D2663 (Ch. 4C1) 11-31

D2665 (Factory 4B114 Series A) 22-31

D2692 39-28

D2709 (Factory No. 470) 27-30

D2710 (Factory No. 24D22-6308R) 23-31

D2718 (Factory No. 227D14-6381U) 2-23

D2743 23-32

D2745 (See Model D1645—Set 6-33)

D2748 (Ch. 7156) 26-27

D2806, D2807 (Factory Model 181) 14-26

D2810 (Factory No. 24D24-7088B) 36-27

D2815 48-25

D2819 (Factory No. 26A82-738) 35-24

D2851 38-28

D2906 (Factory No. 189) 32-28

D2907 69-14

D2910 65-16

D2919 (Fact. No. 6DF21) 59-22

D2963 73-13

D2983 el. Rec. 68-18

D2985 Tel. Rec. 70-11

D2987 Tel. Rec. 69-13

D3120A 203-12

D3130A, B 203-13

D3210A 190-15

D3265A 189-16

D3301 23-26

D3351, D3352, D3353 224-16

D3615 (Factory 25B02-606) 18-32

D3619 (Factory 5P110) 10-33

D3630, D3630N 19-33

D3720 24-29

D3721 (Factory 1108X) 32-28

D3722 (Fact. No. 472) 51-24

D3809 (Factory No. 178) 43-22

D3810 39-27

D3811 (Fact. No. 1148XH) 47-24

D3840 49-26

D4118, B 200-12

D4142A 142-14

D4320 227-15

D4320B 247-13

D-4321 A 229-26

D4650 (Factory No. 5C12) 26-28

D4730 (Factory 26C19-61) 7-28

D4818 (Fact. No. 134XD) 45-26

D4832 (Fact. No. 25C22-82) 47-25

D4842 (Fact. No. 26C21-81) 50-21

D21088A Tel. Rec. 105-11

D21088B Tel. Rec. 145-14

D21089A Tel. Rec. 113-10

D21089B Tel. Rec. 136-14

D21091 Tel. Rec. 161-10

TRUETONE—Cont.

D21093A, D21094A Tel. Rec. 119-12

D21095 Tel. Rec. 134-11

D21185A Tel. Rec. (See Model 2D1185B—Set 154-13)

D21185B Tel. Rec. 154-13

D21185C, D Tel. Rec. (See PCB 43—Set 177-1 and Model 2D1185B—Set 154-13)

D21185E Tel. Rec. (See PCB 43—Set 177-1, PCB 46—Set 180-1 and Model 2D1185B—Set 154-13)

D21190A, B Tel. Rec. 147-12

D21194A Tel. Rec. 151-11

D21230B Tel. Rec. 185-14

D21230C, D, E Tel. Rec. (See PCB 98—Set 243-1 and Model 2D1230B—Set 185-14)

D21230E Tel. Rec. (Also see PCB 59—Set 193-1) 185-14

D21235A (Ch. 17MS345) Tel. Rec. 188-13

D21235B, C, D, E Tel. Rec. (See PCB 74—Set 215-1 and Model 2D1235A—Set 188-13)

D21303A Tel. Rec. 207-11

D21315A Tel. Rec. 204-11

D21316A Tel. Rec. 224-17

D21325A Tel. Rec. 204-11

D21326A Tel. Rec. 224-17

D21330A Tel. Rec. (See PCB 98—Set 243-1 and Model 2D1230B—Set 185-14)

D21331A, B, D Tel. Rec. 233-11

D21331C, D Tel. Rec. (See Model 2D1331A—Set 233-11)

D21336A Tel. Rec. 238-14

D21344A, B (Ch. 21MS36C) Tel. Rec. 210-13

D21352A Tel. Rec. 232-9

D21353A (Series A Thru M) Tel. Rec. 244-12

D21354A (Ch. 9210P) Tel. Rec. 194-13

D21358A Tel. Rec. 242-10

D21359A (Series A, C, D, E) Tel. Rec. 248-10

D21415A (Ch. 21T16) Tel. Rec. 249-19

D21416A (Ch. 21T16A) Tel. Rec. 249-19

D21426A (Ch. 21T16A) Tel. Rec. 249-19

D21430A Tel. Rec. (See PCB 98—Set 185-14 and Model 2D1230B—Set 185-14)

D21430B Tel. Rec. (See Model 2D1430A) 161-10

D22047B Tel. Rec. 161-10

D22049A (Ch. 16AY210) Tel. Rec. 134-11

D22052 Tel. Rec. 4782

D22052A, B (Ch. 16AY210) Tel. Rec. 4780

D22052C (Ch. 17AY23) Tel. Rec. 4800

D22052D, E (Ch. 17AY28) Tel. Rec. 43-23

D22053 Tel. Rec. 120-11

D22149A (Ch. 17AY212) Tel. Rec. 177-14

D22152A (Ch. 17AY26) Tel. Rec. 204-11

D22152B (Ch. 21AY21A) Tel. Rec. 204-11

D22152C (Ch. 21AY21A) Tel. Rec. 204-11

D22301A, D22302A Tel. Rec. 229-17

D22312A Tel. Rec. 204-11

D22313A Tel. Rec. 224-17

D22313C (Ch. 17T5) Tel. Rec. 249-19

D22314A Tel. Rec. 204-11

D22315A Tel. Rec. 224-17

D22321A Tel. Rec. 204-11

D22322A, B Tel. Rec. 203-14

D22333A, B Tel. Rec. 233-11

D22414A (Ch. 21T14) Tel. Rec. 249-19

D2415A (Ch. 21T14A) Tel. Rec. 166

D2422A (Ch. 17T8) Tel. Rec. 181-16

D2422B (Ch. 17T4) Tel. Rec. 288

D2423A Tel. Rec. (See PCB 98—Set 185-14 and Model 2D1230B—Set 185-14)

D2423B (Ch. 17T4) Tel. Rec. 221-12

TURNER

TV-3 Tel. UHF Conv. 231-17

ULTRADYNE

4-21

UNITED MOTORS SERVICE (See Delco or Buick, Cadillac, Chevrolet, Oldsmobile and Pontiac)

U. S. TELEVISION

C16030 Tel. Rec. 99A-12

C16031 Tel. Rec. 99A-12

T1-0823 Tel. Rec. 89-15

T16030 Tel. Rec. 99A-12

T19031 Tel. Rec. 99A-12

5A16, 5B16, 5C16 (See Model 5C66—Set 17-9)

5A66, 5B66, 5C66 5066MPA

5C66 Early 17-9

8-16M (Dumbarton) 26-29

UNITEC

88 5-26

UNIVERSAL CAMERA (See Record Changer Listing)

UTAH (See Record Changer Listing)

V-M (Also see Record Changer Listing)

191-19

110 242-11

150 139-15

150A 213-9

151 231-20

160 187-13

555-M, O 235-13

V-M—Cont.

970 159-15

972 203-15

975 165-16

980 138-12

985 166-16

986 247-14

990 248-11

1001-A 10-34

VAN-CAMP

576-1-6A 7-29

VIDEO CORP. OF AMERICA (See Videola)

VIDEONYE

10FM, 10TV, 12FM, 12TV Tel. Rec. 69-15

VIDEOLA

VS-160, VS-161 Tel. Rec. 92-9

VS-165, VS-166, VS-167, VS-168 Tel. Rec. 92-9

VIDEO PRODUCTS

530-DX Series Tel. Rec. 213-10

630-DXC Tel. Rec. 176-13

630-DX24C Tel. Rec. 176-13

630-K3C Tel. Rec. 176-13

630-K24C Tel. Rec. 176-13

VIETONE

RC-201A, RRC-201 11-32

VISION MASTER

14WC, MT Tel. Rec. (Similar to Chassis) 117-8

16MC, 16MT, 16MXC, 16MXCS, 16MXT, 16MXTS Tel. Rec. (Similar to Chassis) 117-8

17MC, 17MT, 17MXC, 17MXCS, 17MXT, 17MXTS Tel. Rec. (Similar to Chassis) 117-8

VIZ

RS-1 14-31

VOCATRON

CC-20 (D) 246-11

CC-45 247-15

VOGUE

532 A-P 11-33

Ch. Models 533R, 554R 8-32

WARWICK (See Clarion)

WATERSON

ARC-4591A 16-36

MA-4585, APA-4587 3-2

RC-4581 16-35

4581 3-32

4582 34-24

4782 24-31

4780 16-34

4900 43-23

WAVEFORMS

A-20 191-20

C-5 191-20

WEBCOR (See Webster-Chicago)

WEBSTER-CHICAGO (Also see Changer and Recorder Listings)

B-123-1 204-12

B-124-1 203-16

B-134-1 205-12

B-135-1 210-14

B-136-1 207-12

F-123-1 204-12

F-134-1 205-12

F-136-1 207-12

F-137-1 207-12

100-608 121-14

100-621 113-11

129-1, 129-2 215-13

130 119-13

161-1 55-23

181-1R 221-13

288 117-14

333-1, 333-2 250-22

362 105-12

760 112-12

762 102-12

1024 (See Model B-124-1—Set 203-16)

1034 (See Model B-134-1—Set 205-12)

1035 (See Model B-135-1—Set 210-14)

1036 (See Model B-136-1—Set 207-12)

WEBSTER ELECTRIC (Also see Recorder Listing)

81-15, 81-15A 142-15

82-25, 82-25A, 83-25 143-15

84-25 145-12

85-25 144-14

906 100-13

1105M 226-10

WEBSTER (Telehame)

56-24

6066M 57-23

WELLS-GARDNER

3VGS30A8-A-496 246-12

317G534C-218 Tel. Rec. (Also see PCB 84—Set 225-1) 195-12

317G534C-220 Tel. Rec. (Also see PCB 84—Set 225-1) 195-12

317G534C-278 Tel. Rec. (Also see PCB 84—Set 225-1) 195-12

321MS39C-222, -224 Tel. Rec. 194-14

321MS31C-272, -274, -276 Tel. Rec. 194-14

321MS31C-280, -282, 284 Tel. Rec. 194-14

321MS39-322 Tel. Rec. 226-11

321MS39-372-2 Tel. Rec. 226-11

321MS39-376-1 Tel. Rec. 226-11

1321MS31C-296 Tel. Rec. 194-14

2321MS39-324 Tel. Rec. 226-11

2321MS39-370 Tel. Rec. 226-11

2321MS39-396-1 Tel. Rec. 226-11

WESTERN AUTO (See Truetone)

WESTINGHOUSE (Also see Record Changer Listing)

H-104, H-105 4-11

H-104A, H-105A, H-107A, H-108A (See Set 21-36 and Model H-104—Set 4-11)

H-107, H-108, H-110, H-111 4-19

H-113, H-114, H-116 (See Model H-117—Set 11-34)

H-117, H-119 11-34

H-122 6-35

H-122A, B (See Model H-122—Set 6-35)

H-125, H-126 3-19

H-130 54-20

H-133 14-34

H-137 (See Model H-138—Set 6-36)

H-138 6-36

H-147 31-33

H-148 15-37

H-148A (See Model H-148—Set 15-37)

H-153, H-153A (Ch. V-2103) 35-25

H-154 (See Set 21-36 and Model H-104—Set 4-11)

H-155 35-25

H-156 (See Model H-153—Set 35-25)

H-157 (Ch. V-2122) 33-31

H-161 (Ch. V-2118) 34-27

H-162 (See Model H-117—Set 11-34)

H-164 (Ch. V-2119-1) 36-28

H-165 32-29

H-166, H-167 (See Model H-164) 36-28

H-168, H-168A, H-168B (Ch. V-2118) (See Model H-161) 34-27

H-168B (Ch. V-2118) (See Model H-168—Set 34-27)

H-169 (Ch. V-2124-1) 37-24

H-171 (Ch. V-2103) 35-25

H-171A, C (Ch. V-2103) (See Model H-153—Set 35-25)

H-178 (Ch. V-2123) 35-26

H-182 (Ch. V-2128, V-2128-1) 33-25

H-183, H-183A 48-26

H-184 (See Model H-153—Set 35-25)

H-185 (Ch. V-2131, V-2131-1) 35-26

H-186M, H-187 (Ch. V-2132) 60-20

H-188 (Ch. V-2133) 51-25

H-190, H-191, H-191A (Ch. V-2134) 59-23

H-195 54-20

H-196 (Ch. V-2130-1) Tel. Rec. (See Model H-196—Set 65-17)

H-196A (Ch. V-2130-1DX or V-2130-1DX) Tel. Rec. 84-13

H-198 (Ch. V-2137-2) 73-15

H-199 (Ch. V-2137-1) 66-16

H-202 (Ch. V-2128-2) 50-22

H-203 (Ch. V-2137) 62-21

H-204 50-22

H-207A (Ch. V-2130-1, V-2137) Tel. Rec. 65-17

H-207A (DX) (Ch. V-2130-1DX or V-2137) Tel. Rec. 84-13

H-207B (DX) (Ch. V-2130-1DX or V-2130-2DX and Radio Ch. V-2137) Tel. Rec. 84-13

H-210, H-211 (Ch. V-2144) 61-20

H-212 (Ch. V-2137) 62-21

H-214, H-214A (Ch. V-2103-3) 75-16

H-216, H-216A (Ch. V-2146-05, V-2146-45, V-2149-1) Tel. Rec. 97A-14

H-217, A (Ch. V-2146-1DX, V-2137, V-2149) Tel. Rec. (See Set 99A-14 and Model H-217B—Set 91-14)

H-217B (Ch. V-2146-35DX, V-2137, V-2149) Tel. Rec. 91-14

H-220 59-23

H-223 (Ch. V-2150-01, V-2150-02) Tel. Rec. 78-14

H-225 (DX) (Ch. V-2130-3DX or V-2130-3DX) Tel. Rec. 99A-17

H-226 (Ch. V-2146-21DX, -25DX, V-2149) Tel. Rec. (See Model H-217B—Set 91-14)

H-231 (Ch. V-2150-51 and V-2137-3 or V-2137-35, V-2149-2) Tel. Rec. 99A-14

H-242 (Ch. V-2150-31) Tel. Rec. 97A-14

H-251 (Ch. V-2150-81, -82, -84) Tel. Rec. (See 99A-14 and Model H-609T10—Set 95-7)

H-300T5, H-301T5 (Ch. V-2148) 88-14

H-302P5 (Ch. V-2151-1) 91-15

H-303P4, H-304P4 (Ch. V-2153) 89-16

H-307T7, H-308T7 (Ch. V-2136) 91-15

H-309P5, H-309PSU (Ch. V-2156) 101-16

H-310T5, H-310TSU, H-311T5, H-311TSU (Ch. V-2161, V-2161U) 99-18

H-312P4, H-312PAU, H-313P4, H-313PAU, H-315P4U (Ch. V-2153-1) 98-13

H-316C7 (Ch. V-2136-1), H-317C7 (Ch. V-2136-1) (See Model H-316C7—Set 12-13)

H-318T5, U (Ch. V-2157, U) 117-15

H-320T5, U (Ch. V-2157, U) 117-15

H-321T5, U, H-322T5, U (Ch. V-21

WESTINGHOUSE—Cont.

H-331P4, U (Ch. V-2164, U) (Also see PCB 52—Set 186-1) 171-12
H-332P4 (See Model H-331P4—Set 171-12)
H-333P4, U (Ch. V-2164, U) (Also see PCB 52—Set 187-1) 171-12
H-3347U, H-3357U (Ch. V-2136-5U) 142-16
H-3347UR (Ch. V-2136-5U) 149-14
H-33675U, H-33775U (Ch. V-2157L) 134-12
H-33875 (Ch. V-2157-4U) 140-13
H-34175U (Ch. V-2157-4U) 140-13
H-342P5J, H-343P5U (Ch. V-2156-1U) 138-13
H-34575 H34675 (Ch. V-2157-4U) (See Model H-33875—Set 140-13)
H-349P5, H-349P5 (Ch. V-2156-1U) (See Model H-342P5—Set 138-13)
H-35077, H-35177 (Ch. V-2180-1) (Also see PCB 52—Set 186-1) 154-11
H-354C7 (Ch. V-2180-2), 158-13
H-35575, H-35675 (Ch. V-2157-5) 161-11
H-357C10 (Ch. V-2180-5), 161-12
H-35975, H-36075 (Ch. V-2157-6) 191-21
H-36116 (Ch. V-2181-1), 186-15
H-36575, H-36675 (Ch. V-2157-7) 185-15
H-36775 (Ch. V-2157-8), 189-17
H-368P5, H-369P5 (Ch. V-2156-1U) (See Model H-342P5—Set 138-13)
H-37077, H-37177 (Ch. V-2180-8) 186-16
H-372P4, H-373P4, Ch. V-2182-1 and H-377 Optional Pwr. Supply 188-14
H-37475, H-37575 (Ch. V-2157-9) 189-17
H-376P4 (Ch. V-2182-1 and H-377 Optional Power Supply, 188-14
H-377 (Power Supply) (See Set 188-14 or Set 233-12)
H-37875, H-37975, H-38075, H-38175 (Ch. V-2184-1), 211-17
H-38275, H-38375 (Ch. V-2157-10) 212-9
H-38475 (Ch. V-2157-10) (See Model H-38275—Set 215-14)
H-38575, H-38675 (Ch. V-2157-11) 204-13
H-38775 (Ch. V-2157-11) (See Model H-38575—Set 204-13)
H-38875, H-38975 (Ch. V-2157-12) 215-15
H-39175, H-39275 (Ch. V-2157-14) 231-19
H-39375, H-39475 (Ch. V-2181-2), 210-15
H-39775, H-39875 (Ch. V-2184-2) 232-10
H-400P4, H-401P4, H-402P4, H-403P4, Ch. V-2164-2), 205-13
H-40575 (Ch. V-2157-14) (See Model H-39175—Set 231-19)
H-409P4, H-410P4, H-411P4 (Ch. V-2185-3 and H-377 Optional Power Supply), 233-12
H-41775, H-41875 (Ch. V-2186-1) 239-11
H-422P4, H-423P4, H-424P4, H-425P4 (Ch. V-2188-1) 245-11
H-45175, H-45275, H-45375, H-45475 (Ch. V-2184-1) (See Model H-37875—Set 211-17)
H-600T16 (Ch. V-2150-61, A, B) Tel. Rec. 98-14
H-601K17, H-602K12 (Ch. V-2150-41) Tel. Rec. 98-14
H-603C12 (Ch. V-2152-01 and V-2149-3) Tel. Rec. 100-14
H-604T10, A (Ch. V-2150-91A, 94, 94A) Tel. Rec. (See Set 99A-14 and Model H-609T10—Set 95-7)
H-605T12 (Ch. V-2150-101) Tel. Rec. 97-19
H-606K12 (Ch. V-2150-111, A) Tel. Rec. 120-12
H-607K12 (Ch. V-2150-111, A) Tel. Rec. 120-12
H-608C12 (Ch. V-2152-01 and V-2149-3) Tel. Rec. (See Model H-603C-12—Set 100-14)
H-609T10 (Ch. V-2150-94C) Tel. Rec. 95-7
H-610T12 (Ch. V-2150-136) Tel. Rec. 105-13
H-611C12 (Ch. V-2152-16) Tel. Rec. 112-14
H-613K16 (Ch. V-2150-146) Tel. Rec. 107-12
H-614T12 (Ch. V-2150-136) Tel. Rec. 105-13
H-615C12 (Ch. V-2152-16) Tel. Rec. 112-14
H-617T12 (Ch. V-2150-176, U) Tel. Rec. (Also see PCB 10—Set 116-1) 103-17
H-618T16 (Ch. V-2150-186, A, C, CA) Tel. Rec. (Also see PCB 10—Set 115-1) 103-17
H-619T12, J (Ch. V-2150-176, U) Tel. Rec. (Also see PCB 10—Set 116-1) 103-17
H-620K16 (Ch. V-2150-186, A, C, CA) Tel. Rec. (Also see PCB 10—Set 115-1) 103-17
H-622K16 (Ch. V-2150-186, A, C, CA) Tel. Rec. (See PCB 10—Set 116-1 and Model H-617T12—Set 103-17)
H-625T12 (Ch. V-2150-197) Tel. Rec. 114-11
H-626T16 (Ch. V-2172) Tel. Rec. 116-13
H-627K16 (Ch. V-2171) Tel. Rec. 116-13
H-628K16, H-629K16 (Ch. V-2171) Tel. Rec. 116-13
H-630T14 (Ch. V-2176) Tel. Rec. 116-13
H-633C17, H-634C17 (Ch. V-2173) Tel. Rec. 122-11
H-636T17 (Ch. V-2175) Tel. Rec. 116-13

WESTINGHOUSE—Cont.

H-637T14 (Ch. V-2177) Tel. Rec. 116-13
H-638K20 (Ch. V-2178) Tel. Rec. 129-13
H-639T17 (Ch. V-2192, -1) Tel. Rec. 133-15
H-640T17 (Ch. V-2192, -2, -3, -4, -5, -6) Tel. Rec. (Also see PCB 28—Set 150-1) 133-15
H-641K17 (Ch. V-2175-1, -5), H-641K17A (Ch. V-2192, -1, -2, -3, -4, -5, -6) Tel. Rec. (Also see PCB 28—Set 150-1) 133-15
H-642K20A (Ch. V-2194, V-2194A, V-2194-1) Tel. Rec. 137-16
H-643K16 (Ch. V-2179, V-2179-1) Tel. Rec. 127-13
H-646K17 (Ch. V-2192) Tel. Rec. 133-15
H-647K17 (Ch. V-2175-3) Tel. Rec. 133-15
H-648T20 (Ch. V-2201-1) Tel. Rec. (Also see PCB 42—Set 175-1) 154-15
H-649T17 (Ch. V-2200-1) Tel. Rec. (Also see PCB 42—Set 175-1) 154-15
H-649T17 (Ch. V-2192-4) Tel. Rec. (See Model H-639T17—Set 133-15)
H-650K21 (Ch. V-2192-4) Tel. Rec. (See Model H-639T17—Set 133-15)
H-650T17 (Ch. V-2200-1) Tel. Rec. (Also see PCB 42—Set 176-1) 154-15
H-651K17 (Ch. V-2192) Tel. Rec. (See Model H-639T17—Set 133-15)
H-651K17 (Ch. V-2200-1) Tel. Rec. (Also see PCB 42—Set 176-1) 154-15
H-652K20 (Ch. V-2194-2, -3) Tel. Rec. (See PCB 31—Set 157-3 and Model H-642K20A—Set 137-16)
H-652K20 (Ch. V-2201-1) Tel. Rec. (Also see PCB 42—Set 176-1) 154-15
H-653K24 (Ch. V-2202-2, V-2210-1) Tel. Rec. (Also see PCB 35—Set 164-1) 160-13
H-654T17 (Ch. V-2175-3, -4, V-2192, -1) Tel. Rec. 133-15
H-655K17, H-656K17, H-657K17 (Ch. V-2200-1) Tel. Rec. (Also see PCB 42—Set 176-1) 154-15
H-657K17 (Ch. V-2192-4, -5, -6) Tel. Rec. (See PCB 28—Set 150-1 and Model H-639T17—Set 133-15)
H-658T17 (Ch. V-2192, -1) Tel. Rec. (See PCB 28—Set 150-1 and Model H-639T17—Set 133-15)
H-659T17 (Ch. V-2204-1) Tel. Rec. (Also see PCB 42—Set 176-1) 154-15
H-660C17, H-661C17 (Ch. V-2203-1 and Radio Ch. V-2180-3) Tel. Rec. (Also see PCB 46—Set 180-1) 157-12
H-662K20 (Ch. V-2201-1) Tel. Rec. (Also see PCB 42—Set 176-1) 154-15
H-663T17 (Ch. V-2192-2) Tel. Rec. (See PCB 28—Set 150-1 and Model H-639T17—Set 133-15)
H-663T17 (Ch. V-2204) Tel. Rec. (Also see PCB 42—Set 177-1) 154-5
H-664K17 (Ch. V-2200-1) Tel. Rec. (Also see PCB 42—Set 176-1) 154-15
H-665T16 (Ch. V-2204-1) Tel. Rec. (See PCB 42—Set 176-1 and Model H-648T20—Set 154-15)
H-667T17, H-668T17 (Ch. V-2216) Tel. Rec. (Also see PCB 40—Set 172-1) 167-15
H-673K21 (Ch. V-2217-1) Tel. Rec. (See Model H-667T17—Set 167-15)
H-676T21 (Ch. V-2217-1) Tel. Rec. (See Model H-667T17—Set 167-15)
H-678K17, H-679K17 (Ch. V-2216-1, -2, -3) Tel. Rec. (Also see PCB 40—Set 172-1, PCB 45—Set 179-1 and PCB 52—Set 186-1) 167-15
H-681T17 (Ch. V-2215-1) Tel. Rec. (See PCB 45—Set 179-1, PCB 52—Set 186-1 and Model H-667T17—Set 167-15)
H-688K24 (Ch. V-2219-1) (Also see PCB 52—Set 186-1) 174-14
H-689T16 (Ch. V-2214-1) (See PCB 40—Set 172-1, PCB 52—Set 186-1 and Model H-667T17—Set 167-15)
H-690K21, H-691K21 (Ch. V-2217-1) Tel. Rec. (See Model H-667T17—Set 167-15)
H-692T17 (Ch. V-2217-2, -3) Tel. Rec. (See PCB 43—Set 177-1, PCB 52—Set 186-1 and Model H-667T17—Set 167-15)
H-695K21 (Ch. V-2217-2, -3) Tel. Rec. (See PCB 43—Set 177-1, PCB 52—Set 186-1 and Model H-667T17—Set 167-15)
H-699K17 (Ch. V-2216-2, -3) Tel. Rec. (See PCB 40—Set 172-1, PCB 45—Set 179-1, PCB 52—Set 186-1 and Model H-667T17—Set 167-15)
H-700T17, H-701T17 (Ch. V-2216-2, -3) Tel. Rec. (See PCB 40—Set 172-1, PCB 45—Set 179-1, PCB 52—Set 186-1 and Model H-667T17—Set 167-15)
H-701K21 (Ch. V-2217-2) Tel. Rec. (See PCB 43—Set 177-1 and Model H-667T17—Set 167-15)

WESTINGHOUSE—Cont.

H-702K17, H-703K17 (Ch. V-2216-2, -3) Tel. Rec. (See PCB 40—Set 172-1, PCB 45—Set 179-1, PCB 52—Set 186-1 and Model H-667T17—Set 167-15)
H-704T17 (Ch. V-2216-2, -3) Tel. Rec. (See PCB 40—Set 172-1, PCB 45—Set 179-1, PCB 52—Set 186-1 and Model H-667T17—Set 167-15)
H-704T17 (Ch. V-2216-4, -5) Tel. Rec. 202-10
H-705K17 (Ch. V-2216-2, -3) Tel. Rec. (See PCB 40—Set 172-1, PCB 45—Set 179-1, PCB 52—Set 186-1 and Model H-667T17—Set 167-15)
H-706T16 (Ch. V-2207-1) Tel. Rec. 193-12
H-708T20 (Ch. V-2220-1, -3, -11) Tel. Rec. 193-12
H-710T21 (Ch. V-2217-2, -3) Tel. Rec. (See PCB 40—Set 172-1, PCB 43—Set 177-1, PCB 43—Set 177-1, PCB 52—Set 186-1 and Model H-667T17—Set 167-15)
H-710T21 (Ch. V-2217-4, -5) Tel. Rec. 202-10
H-711T21 (Ch. V-2217-2, -3) Tel. Rec. (See PCB 40—Set 172-1, PCB 43—Set 177-1, PCB 52—Set 186-1 and Model H-667T17—Set 167-15)
H-711T21 (Ch. V-2217-4, -5) Tel. Rec. 202-10
H-713K21 (Ch. V-2217-2, -3) Tel. Rec. (See PCB 40—Set 172-1, PCB 43—Set 177-1, PCB 52—Set 186-1 and Model H-667T17—Set 167-15)
H-714K21 (Ch. V-2217-2, -3) Tel. Rec. (See PCB 40—Set 172-1, PCB 43—Set 177-1, PCB 52—Set 186-1 and Model H-667T17—Set 167-15)
H-714K21 (Ch. V-2217-4, -5) Tel. Rec. 202-10
H-715K21 (Ch. V-2217-2, -3) Tel. Rec. (See PCB 40—Set 172-1, PCB 43—Set 177-1, PCB 52—Set 186-1 and Model H-667T17—Set 167-15)
H-715K21 (Ch. V-2217-4, -5) Tel. Rec. 202-10
H-718K20 (Ch. V-2220-2) Tel. Rec. 193-12
H-720K21 (Ch. V-2217-2, -3) Tel. Rec. (See PCB 40—Set 172-1, PCB 43—Set 177-1, PCB 52—Set 186-1 and Model H-667T17—Set 167-15)
H-720K21 (Ch. V-2217-4, -5) Tel. Rec. 202-10
H-721K21 (Ch. V-2217-2, -3) Tel. Rec. (See PCB 40—Set 172-1, PCB 43—Set 177-1, PCB 52—Set 186-1 and Model H-667T17—Set 167-15)
H-721K21 (Ch. V-2217-4, -5) Tel. Rec. 202-10
H-722K21 (Ch. V-2217-2, -3) Tel. Rec. (See PCB 40—Set 172-1, PCB 43—Set 177-1, PCB 52—Set 186-1 and Model H-667T17—Set 167-15)
H-722K21 (Ch. V-2217-4, -5) Tel. Rec. 202-10
H-723K21 (Ch. V-2217-2, -3) Tel. Rec. (See PCB 40—Set 172-1, PCB 43—Set 177-1, PCB 52—Set 186-1 and Model H-667T17—Set 167-15)
H-723K21 (Ch. V-2217-4, -5) Tel. Rec. 202-10
H-724T20, H-725T20 (Ch. V-2220-2) Tel. Rec. 193-12
H-730C21 (Ch. V-2218-1 and Radio Ch. V-2180-9, -10) Tel. Rec. 190-16
H-730C21 (Ch. V-2218-2 and Radio Ch. V-2180-9, -10) Tel. Rec. (Also see PCB 59—Set 193-1) 190-16
H-732C21 (Ch. V-2218-1 and Radio Ch. V-2180-9, -10) Tel. Rec. 190-16
H-732C21 (Ch. V-2218-1 and Radio Ch. V-2180-9, -10) Tel. Rec. (Also see PCB 59—Set 193-1) 190-16
H-733C21 (Ch. V-2218-1 and Radio Ch. V-2180-9, -10) Tel. Rec. 190-16
H-733C21 (Ch. V-2218-1 and Radio Ch. V-2180-9, -10) Tel. Rec. (Also see PCB 59—Set 193-1) 190-16
H-735T17 (Ch. V-2227-1) Tel. Rec. (Also see PCB 89—Set 333-1) 214-10
H-737T17 (Ch. V-2216-5) Tel. Rec. 202-10
H-737T17 (Ch. V-2232-2) Tel. Rec. 212-9
H-738T17 (Ch. V-2227-1) Tel. Rec. (Also see PCB 89—Set 333-1) 214-10
H-739T17, H-739T17 (Ch. V-2227-2) Tel. Rec. 214-10
H-740T21, H-742K21, H-743K21 (Ch. V-2233-1) Tel. Rec. (Also see Prod. Chg. Bul. 99—Set 244-1) 212-9
H-744K21, H-744K21, H-747K21, H-747K21 (Ch. V-2233-4) Tel. Rec. 215-16
H-750T21 (Ch. V-2233-3) Tel. Rec. 212-9
H-751T21 (Ch. V-2217-4, -5) Tel. Rec. 202-10
H-751T21 (Ch. V-2233-2) Tel. Rec. 212-9
H-752T21 (Ch. V-2217-4, -5) Tel. Rec. 202-10
H-752T21 (Ch. V-2233-2) Tel. Rec. 212-9
H-753K21 (Ch. V-2233-3) Tel. Rec. 212-9

WESTINGHOUSE—Cont.

H-754K21 (Ch. V-2217-4, -5) Tel. Rec. 202-10
H-754K21 (Ch. V-2233-2) Tel. Rec. 212-9
H-755K21 (Ch. V-2233-2) Tel. Rec. 212-9
H-756K21 (Ch. V-2217-4, -5) Tel. Rec. 202-10
H-756K21 (Ch. V-2233-2) Tel. Rec. 212-9
H-757K21 (Ch. V-2217-4, -5) Tel. Rec. 202-10
H-757K21 (Ch. V-2233-2) Tel. Rec. 212-9
H-758K21 (Ch. V-2217-4, -5) Tel. Rec. 202-10
H-758K21 (Ch. V-2233-2) Tel. Rec. 212-9
H-759K21 (Ch. V-2217-4, -5) Tel. Rec. 202-10
H-759K21 (Ch. V-2233-2) Tel. Rec. 212-9
H-760T21 (Ch. V-2233-2) Tel. Rec. 212-9
H-760T21 (Ch. V-2233-2) Tel. Rec. 212-9
H-761T21 (Ch. V-2233-2) Tel. Rec. 212-9
H-761T21 (Ch. V-2233-2) Tel. Rec. 212-9
H-795T27, H-795T27 (Ch. V-2250-1) Tel. Rec. 241-12
H-802 (Ch. V-11900-1, -2, -3, -4, -5, V-11213) Tel. UHF Conv. 209-13
H-815T24, H-815T24 (Ch. V-2250-1) Tel. Rec. 241-12
H-817K24, H-817K24 (Ch. V-2250-1) Tel. Rec. 241-12
H-1251 (See Model H-104)
Ch. V-2102 (See Model H-104)
Ch. V-2102-1 (See Model H-138)
Ch. V-2103 (See Model H-153)
Ch. V-2103-3 (See Model H-214)
Ch. V-2107 (See Model H-133)
Ch. V-2118 (See Model H-161)
Ch. V-2119 (See Model H-164)
Ch. V-2120 (See Model H-161)
Ch. V-2122 (See Model H-157)
Ch. V-2123 (See Model H-178)
Ch. V-2124 (See Model H-169)
Ch. V-2127 (See Model H-183)
Ch. V-2128, V-2128-1 (See Model H-182)
Ch. V-2128-2 (See Model H-202)
Ch. V-2130-1 (See Model H-196)
Ch. V-2130-1DX, -1DX [See Model H-196A (DX)]
Ch. V-2130-2DX, -2DX [See Model H-207A (DX)]
Ch. V-2130-3DX, 3DX [See Model H-225 (DX)]
Ch. V-2131, V-2131-1 (See Model H-185)
Ch. V-2132 (See Model H-186M)
Ch. V-2133 (See Model H-188)
Ch. V-2134 (See Model H-190)
Ch. V-2136 (See Model H-3077)
Ch. V-2136-1 (See Model H-316C7)
Ch. V-2136-2 (See Model H-3247)
Ch. V-2136-4 (See Model H-328C7)
Ch. V-2136-5R (See Model H-3347U)
Ch. V-2137-5U (See Model H-3347U)
Ch. V-2137 (See Model H-203)
Ch. V-2137-1 (See Model H-199)
Ch. V-2137-2 (See Model H-198)
Ch. V-2137-3, V-2137-3S (See Model H-231)
Ch. V-2144, V-2144-1 (See Model H-210)
Ch. V-2146-05 (See Model H-216)
Ch. V-2146-1DX (See Model H-217)
Ch. V-2146-2DX, -25DX (See Model H-226)
Ch. V-2146-35DX (See Model H-217)
Ch. V-2146-45 (See Model H-216)
Ch. V-2148 (See Model H-200T5)
Ch. V-2149 (See Model H-217)
Ch. V-2149-1 (See Model H-216)
Ch. V-2149-2 (See Model H-231)
Ch. V-2149-3 (See Model H-603C-12)
Ch. V-2150-01, V-2150-02 (See Model H-223)
Ch. V-2150-31 (See Model H-242)
Ch. V-2150-41 (See Model H-601K-12)
Ch. V-2150-51 (See Model H-231)
Ch. V-2150-61, A, B (See Model H-600T16)
Ch. V-2150-81, -82, -84 (See Model H-251)
Ch. V-2150-91A (See Model H-604-T10, A)
Ch. V-2150-94 (See Model H-609T10)
Ch. V-2150-101 (See Model H-605T12)
Ch. V-2150-111, A (See Model H-606K12)
Ch. V-2150-136 (See Model H-610T12)
Ch. V-2150-146 (See Model H-613K16)
Ch. V-2150-176, U (See Model H-617T12)
Ch. V-2150-177U (See Model H-617T12)
Ch. V-2150-186, A, C, CA (See Model H-619T12)
Ch. V-2150-197 (See Model H-625T12)
Ch. V-2151-1 (See Model H-302P5)
Ch. V-2152-01 (See Model H-603C-12)
Ch. V-2152-16 (See Model H-615C12)
Ch. V-2153 (See Model H303P4)
Ch. V-2153-1 (See Model H-312P4)
Ch. V-2156 (See Model H-309P5)
Ch. V-2156-1U (See Model H-342-PSU)

WESTINGHOUSE—Cont.

Ch. V-2157, U (See Model H-318T5)
Ch. V-2157-1, -1U (See Model H-321T5)
Ch. V-2157-2, -2U (See Model H-323T5)
Ch. V-2157-3U (See Model H-327T5U)
Ch. V-2157-4U (See Model H338-T5U)
Ch. V-2157-5 (See Model H-355T5)
Ch. V-2157-6 (See Model H-359T5)
Ch. V-2157-8 (See Model H-367T5)
Ch. V-2157-9 (See Model H-374T5)
Ch. V-2157-10 (See Model H-382T5)
Ch. V-2157-11 (See Model H-385T5)
Ch. V-2157-12 (See Model H-388T5)
Ch. V-2157-14 (See Model H-391T5)
Ch. V-2161, V-2161U (See Model H-310T5)
Ch. V-2164, U (See Model H-331P4)
Ch. V-2164-2 (See Model H-400P4)
Ch. V-2172 (See Model H-627K16)
Ch. V-2172-5 (See Model H-626T16)
Ch. V-2173 (See Model H-633C17)
Ch. V-2175 (See Model H-636T17)
Ch. V-2175-1 (See Model H-641-K17)
Ch. V-2175-3, -4 (See Model H-640T17)
Ch. V-2175-5 (See Model H-641K17)
Ch. V-2175-6 (See Model H-630T14)
Ch. V-2177 (See Model H-637T14)
Ch. V-2178, -1, -3 (See Model H-638K20)
Ch. V-2180-1 (See Model H350T7)
Ch. V-2180-2 (See Model H-354C7)
Ch. V-2180-3 (See Model H-660C17)
Ch. V-2180-5 (See Model H-357C10)
Ch. V-2180-9 (See Model H-370T7)
Ch. V-2180-9, -10 (See Model H-739T17)
Ch. V-2181-1 (See Model H-361T6)
Ch. V-2181-2 (See Model H-393T6)
Ch. V-2184-1 (See Model H-378T5)
Ch. V-2184-2 (See Model H-397T5)
Ch. V-2185-1 (See Model H-409P4)
Ch. V-2186-1 (See Model H-417T5)
Ch. V-2188-1 (See Model H-422P4)
Ch. V-2192, -1 (See Model H-639T17)
Ch. V-2192, -3, -4, -5, -6 (See Model H-640T17)
Ch. V-2194, V-2194A, V-2194-1 (See Model H-642K20A)
Ch. V-2194-2, -3 (See Model H-652K20)
Ch. V-2200-1 (See Model H-651-K17)
Ch. V-2202-1 (See Model H-652-K20)
Ch. V-2202-2 (See Model H-653K24)
Ch. V-2203-1 (See Model H-660C17)
Ch. V-2204-1 (See Model H-659T17)
Ch. V-2206-1 (See Model H-665T16)
Ch. V-2207-1 (See Model H-705T16)
Ch. V-2210-1 (See Model H-653K24)
Ch. V-2214-1 (See Model H-689T16)
Ch. V-2215-1 (See Model H-681T17)
Ch. V-2216-1 (See Model H-657T17)
Ch. V-2216-2, -3 (See Model H-678K17)
Ch. V-2216-4, -5 (See Model H-704T17)
Ch. V-2217-1 (See Model H-673K21)
Ch. V-2217-2, -3 (See Model H-692T17)
Ch. V-2217-4, -5 (See Model H-710T21)
Ch. V-2218-1, 2, 11 (See Model H-730C21)
Ch. V-2218-1 (See Model H-688K24)
Ch. V-2220-1 (See Model H-708T20)
Ch. V-2220-2 (See Model H-718K20)
Ch. V-2220-3, -11 (See Model H-708T20)
Ch. V-2227-1 (See Model H-736T17)
Ch. V-2227-2 (See Model H-739T17)
Ch. V-2232-2 (See Model H-737T17)
Ch. V-2233-1 (See Model H-704T17)
Ch. V-2233-2 (See Model H-751T21)
Ch. V-2233-3 (See Model H-750T21)
Ch. V-2233-4 (See Model H-746K21)
Ch. V-2250-1 (See Model H-795T27)
Ch. V-11213 (See Model H-802)
Ch. V-11900-1, -2, -3, -4, -5 (See Model H-802)
WILCOX-GAY (Also see Majestic) (Also see Recordia)
G-306, G-402, G-403, G-404 Tel. Rec. (See Model H-1272—Set 108-7)
G-414 Tel. Rec. (See Majestic Model G-414—Set 133-8)
G-426, G-427 Tel. Rec. (See Majestic Model 1272—Set 108-7)
G-614, G-624 Tel. Rec. (See Majestic Model G-414—Set 133-8)
G-914 Tel. Rec. (See Majestic Model G-414—Set 133-8)
OD-446M (OD Series) Tel. Rec. 101-17
OF439-1-C (Ch. OF Series) Tel. Rec. 98-15
OD Series (See Model OD-446M) 400A, B, C 242-12

NOTE: PCB denotes Production Change Bulletin

ADDITIONAL PHOTOFAC T BENEFITS

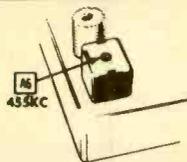
From time to time, PHOTOFAC T Folder Sets include valuable "bonus" aids, as well as useful data of a special nature. The fol-

lowing materials are extra benefits incorporated in the PHOTOFAC T Folder Sets indicated, at no additional cost.

	Set No.		Set No.
1—RETMA Production Source Code (Jan. 1, 1954).....	246	8—Replacement of Disc & Plate Type Ceramic Capacitors.....	68
2—TRADE DIRECTORY—Parts Manufacturers.....	12	9—Certificate entitling subscriber to PHOTOFAC T Volume Labels for Vols. 1-10.....	62
3—National Electrical Code on Antennas.....	88	10—Certificate entitling subscriber to PHOTOFAC T Volume Labels for Vols. 11-20.....	102
4—Record Changer Cross Reference by Manufacturer and Model.....	118	11—Alliance Model ATR Rotator.....	216
5—Mica Capacitor Color Codes.....	48	12—Alliance Model DIR Rotator.....	240
6—Ion Trap Alignment.....	62	13—Alliance Model F-4 Rotator.....	250
7—"Let's Look at the Sync Pulses".....	64	14—Alliance Model HIR Rotator.....	242
		15—Photofact Television Course appearing serially in.....	38-51, 54
		16—CR Tube Dimension Chart.....	112
		17—CR (Electromagnetic) Tube Characteristics Chart.....	112
		18—CR Tube Interchangeability Chart.....	112
		19—NPA maintenance and repair information.....	130
		20—General Electric Clock Data.....	160

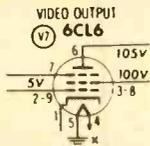
NEW FEATURES MAKE PHOTOFAC T

more useful than ever
for faster, more profitable servicing



Alignment Frequencies

right on photos adjacent to adjustment number—to speed up adjustment.



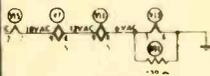
Voltages on Schematics

to help speed voltage analysis for quick location of trouble.



Waveforms on Schematics

reproduced right on the diagram at vital points for rapid analysis by 'scope.



Series Filament Schematic

for quick reference when receiver employs series or series-parallel combination filament string.



Blank Pin or Locating Key

shown on each tube in placement chart (top view) to aid in substituting and replacing tubes without chassis removal.

NEW "EXTRAS"

- Tube types on chassis top photo views
- Tube failure check chart in TV Folders
- Fuse location on tube placement chart
- TV Trouble-Shooting Aids Chart
- Tips on TV servicing in the field
- Color code on transformer leads

for these and hundreds of other good reasons . . .

the men who know

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get PHOTOFAC T regularly
at your Parts Distributor
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Indianapolis 5, Indiana

When the profile of the Cadillac looked like this



It was understandable that the profile of a V.O.M. might look like this



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STREAMLINING signifies the difference!

In cars, streamlining symbolizes the tremendous advances in automotive engineering and performance. In fine test equipment, too, streamlining signifies the difference.

The flush switches, dials and jacks of the Smoothie make it easy to slip in your pocket, carrying case or tool kit, eliminate snag hazards on your tENCH.

But even more—the streamlining expresses externally the advanced internal design which makes the Triplet Model 630 as superior to the obsolete knobby bumpy-faced testers as the Cadillac of today is to the Cadillac of fifty years ago. These internal design features include such developments as selector switch of molded construction, completely enclosed; elimination of harness wiring, etc. Your most frequently used tester—your V.O.M.—should be the best—the one of which many thousands are in use in laboratories today—the Smoothie, Triplet Model 630 Volt-Ohm-Mil-Ammeter, \$39.50 net. Ask your parts jobber or write Triplet Electrical Instrument Company, Bluffton, Ohio.

Only Triplet offers you a ten day free trial on all test equipment.

the SMOOTHIE

the only streamlined V.O.M. with a smooth face

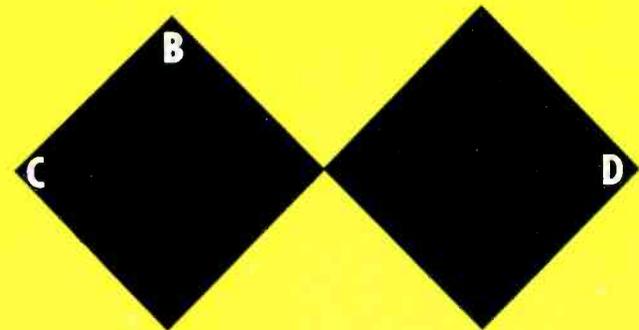
TRIPLETT

630

Volt-Ohm-Mil-Ammeter



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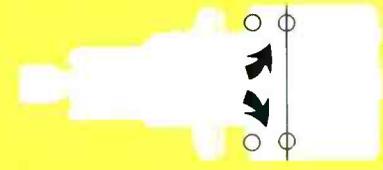


THINGS ARE **NOT** AS THEY SEEM...

The distance AB is the same as the distance CD.



This fuse post is waterproofed to Signal Corp specifications by the addition of the sealing "O" rings indicated.



This fuse post lacking the "O" rings is for general purpose applications.



These two fuse extractor posts look alike
BUT they are not

LITTELFUSE, INC.
DES PLAINES, ILLINOIS