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JUNE 1987

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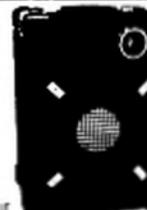
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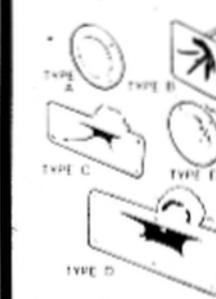
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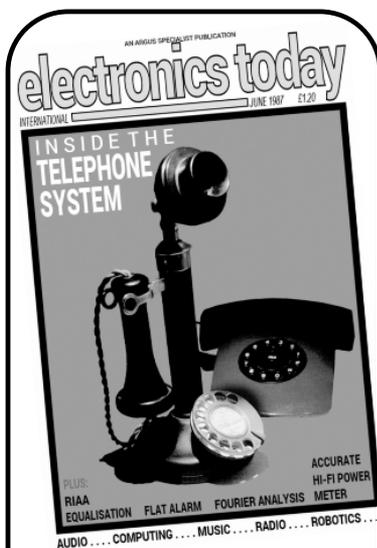
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WS3000 V22bis2400 (as above plus 2400 baud full duplex)..... £650 (b)

**MIRACLE 2000**  
A world standard modem covering V21, V23 (Bell 103/113/108 outside UK) and including 75, 300, 600, 1200 baud ratings. Optional Auto dial, auto answer cards, complete control from computer keyboard. WS2000 £95 c

**GEC DATACHAT 1223:**  
BAPT approved modem complying with CCITT V23 standard. Supplied with software..... £69 (b)

Data Cables for above modems available for most computers.



## SPECIAL OFFER

2764-25	£2.00
27128-25	£2.50
6264LP-15	£3.40

## ATTENTION

All prices in this double page advertisement are subject to change without notice.

**ALL PRICES EXCLUDE VAT**  
Please add carriage 50p unless indicated as follows:  
(a) £8 (b) £2.50 (c) £1.50 (d) £1.00

### Serial Test Cable

Serial Cable switchable at both ends allowing pin options to be re-routed or linked at either end using a 10 way switch making it possible to produce almost any cable configuration on site.  
Available as M/M or M/F      £24.75 (d)

### Serial Mini Patch Box

Allows an easy method to reconfigure pin functions without rewiring the cable assembly.  
Jumpers can be used and reused.      £22 (d)

### Serial Mini Test

Monitors RS232C and CCITT V24 Transmissions, indicating status with dual colour LEDs on 7 most significant lines.  
Connects in Line.      £22.50 (d)

## GANG OF EIGHT INTELLIGENT FAST EPROM COPIER

Copies up to eight eproms at a time and accepts all single rail eproms up to 27256. Can reduce programming time by 80% by using manufacturer's suggested algorithms. Fixed Vpp of 21 & 25 volts and variable Vpp factory set at 12.5 volts. LCD display with alpha moving message. £395(b).

## SOFTY II

This low cost intelligent eprom programmer can program 2716, 2516, 2532, 2732, and with an adaptor, 2564 and 2764. Displays 512 byte page on TV - has a serial and parallel I/O routines. Can be used as an emulator, cassette interface. Softy II..... £195 (b)  
Adaptor for 2764/2564. £25.00 (c)

## UV ERASERS

All erasers with built in safety switch and mains indicator.  
UV1 B erases up to 6 eproms at a time..... £47 (c)  
UV1 A as above but with a timer..... £59 (c)  
UV140 erases up to 14 eproms at a time..... £88 (b)  
UV141 as above but with a timer..... £88 (b)

## CONNECTOR SYSTEMS

### I.D. CONNECTORS

(Speedblock Type)			
No of ways	Header	Recep- tacle	Edge Conn.
10	90p	85p	120p
20	145p	125p	185p
26	175p	150p	240p
34	200p	180p	320p
40	220p	190p	340p
50	235p	200p	390p

### D CONNECTORS

No of Ways      9      15      25      37

<b>MALE:</b>				
Ang Pins	120	180	230	350
Solder	60	85	125	170
IDC	175	275	325	-

<b>FEMALE:</b>				
St Pin	100	140	210	380
Ang pins	160	210	275	440
Solder	90	130	195	290
IDC	195	325	375	-
St Hood	90	95	100	120
Screw	130	150	175	-
Lock	-	-	-	-

### TEXT TOOL ZIF

SOCKETS	24-pin	£7.50
28 pin	40-pin	£12

### EDGE CONNECTORS

2 x 6-way (commodore)	0.1"	0.156"	300p
2 x 10-way			150p
2 x 12-way (vic 20)			350p
2 x 18-way			140p
2 x 23-way (ZX61)			175p
2 x 25-way			225p
2 x 28-way (Spectrum)			200p
2 x 36-way			250p
1 x 43-way			280p
2 x 22-way			190p
2 x 43-way			395p
1 x 77-way			400p
2 x 50-way (S100conn)			600p

### EURO CONNECTORS

DIN 41612		Plug	Socket
2 x 32 way St Pin	230p	275p	
2 x 32 way Ang Pin	275p	320p	
3 x 32 way St Pin	260p	300p	
3 x 32 way Ang Pin	375p	400p	
IDC Skt A + B		400p	
IDC Skt A + C		400p	
For 2 x 32 way please specify spacing (A + B, A + C).			

### MISC CONNS

21 pin Scart Connector	200p
8 pin Video Connector	200p

### AMPHENOL CONNECTORS

Solder		ZDC
36 way plug	500p	475p
36 way skt	550p	500p
24 way plug		
IEEE	475p	475p
24 way skt		
IEEE	500p	500p
PCB Mig Skt Ang Pin		
24 way 700p		38way 750p

### GENDER CHANGERS

25 way D type	
Male to Male	£10
Male to Female	£10
Female to Female	£10

### RS 232 JUMPERS

(25 way D)	
24" Single end Male	
24" Single end Female	
24" Female Female	
24" Male Male	
24" Male Female	

### RIBBON

(grey/metre)			
10-way	40p	34-way	160p
16-way	60p	40-way	180p
20-way	85p	50-way	200p
26-way	120p	64-way	280p

### DIL HEADERS

Solder		IDC
14 pin	40p	100p
16 pin	50p	110p
18 pin	80p	
20 pin	75p	
24 pin	100p	150p
28 pin	160p	200p
40 pin	200p	225p

## TECH NOLINE VIEWDATA SYSTEM

Using 'Prestel' type protocols for information and orders phone 01-450 9764. 24 hour service, 7 days a week.

74 SERIES		74181	340p	74LS162A	75p	74S08	60p	4063	65p
7400	30p	74182	140p	74LS163A	75p	74S10	60p	4066	40p
7401	30p	74184	180p	74LS164	75p	74S11	75p	4067	230p
7402	30p	74185A	180p	74LS165A	110p	74S20	60p	4068	25p
7403	30p	74190	130p	74LS166A	150p	74S22	60p	4069	24p
7404	36p	74191	130p	74LS166B	150p	74S23	60p	4070	24p
7405	30p	74192	110p	74LS167	100p	74S24	60p	4071	24p
7406	30p	74193	115p	74LS170	100p	74S25	60p	4072	24p
7407	30p	74194	110p	74LS173A	100p	74S28	60p	4073	24p
7408	30p	74195	80p	74LS174	75p	74S29	60p	4074	24p
7409	30p	74196	130p	74LS175	75p	74S30	60p	4075	24p
7410	30p	74197	110p	74LS181	200p	74S31	60p	4076	25p
7411	30p	74198	220p	74LS183	100p	74S32	60p	4077	25p
7412	30p	74221	220p	74LS190	75p	74S35	300p	4081	24p
7413	60p	74251	110p	74LS191	75p	74S36	100p	4082	25p
7414	70p	74252	150p	74LS192	100p	74S37	150p	4085	50p
7415	70p	74253	150p	74LS193	100p	74S38	150p	4086	50p
7416	36p	74254	380p	74LS194A	75p	74S39	120p	4089	75p
7417	40p	74273	200p	74LS195A	75p	74S40	120p	4093	35p
7420	30p	74276	100p	74LS196	80p	74S43	100p	4094	80p
7421	60p	74278	170p	74LS197	80p	74S44	100p	4095	80p
7422	36p	74279	80p	74LS221	80p	74S48	100p	4096	80p
7423	36p	74283	105p	74LS240	80p	74S49	100p	4097	270p
7425	40p	74285	320p	74LS241	80p	74S50	100p	4098	75p
7426	40p	74290	80p	74LS242	80p	74S51	100p	4099	80p
7427	40p	74293	80p	74LS243	80p	74S52	150p	4501	36p
7428	43p	74298	80p	74LS244	80p	74S53	150p	4502	53p
7430	30p	74351	200p	74LS245	110p	74S54	200p	4503	36p
7432	36p	74365A	80p	74LS247	110p	74S55	200p	4504	65p
7433	30p	74368A	80p	74LS248	110p	74S56	380p	4505	380p
7437	30p	7436A	80p	74LS249	110p	74S57	60p	4506	60p
7438	40p	74378A	80p	74LS251	75p	74S58	60p	4507/4030	
7439	40p	74368A	70p	74LS253	75p	74S59	320p		
7440	40p	74376	180p	74LS256	80p	74S175	100p	4508	120p
7441	60p	74390	110p	74LS257A	70p	74S188	100p	4510	55p
7442	70p	74393	112p	74LS258A	70p	74S190	300p	4511	55p
7443A	100p	74490	140p	74LS259	120p	74S196	300p	4512	150p
7444	100p			74LS260	75p	74S197	350p	4513	150p
7448A	100p			74LS261	120p	74S200	400p	4514	110p
7447A	100p			74LS268	80p	74S201	350p	4515	110p
7448	120p			74LS273	125p	74S205	80p	4516	55p
7450	36p			74LS279	150p	74S240	400p	4517	220p
7451	36p			74LS280	180p	74S241	400p	4518	48p
7453	36p			74LS283	80p	74S244	600p	4519	32p
7454	36p			74LS284	80p	74S245	250p	4520	80p
7455	36p			74LS290	80p	74S251	250p	4521	115p
7456	36p			74LS292	80p	74S252	250p	4522	80p
7458	40p			74LS293	80p	74S258	250p	4522	80p
7470	60p			74LS295	140p	74S280	100p	4526	70p
7472	65p			74LS300	150p	74S281	300p	4527	80p
7473	65p			74LS311	240p	74S283	270p	4528	65p
7474	60p			74LS312	240p	74S287	225p	4529	100p
7475	60p			74LS313	370p	74S288	200p	4531	75p
7476	45p			74LS314	360p	74S323	225p	4532	65p
7480	65p			74LS315	240p	74S324	500p	4534	380p
7481	180p			74LS320	240p	74S337	400p	4536	250p
7483A	105p			74LS321	240p	74S352	120p	4538	75p
7484A	125p			74LS322	240p	74S353	120p	4538	75p
7485	110p			74LS324	80p	74S356	210p	4541	80p
7488	40p			74LS326	240p	74S383	180p	4543	70p
7489	210p			74LS327	240p	74S384	180p	4551	100p
7490A	85p			74LS328	240p	74S385	180p	4553	240p
7491	70p			74LS330	240p	74S386	80p	4555	36p
7492A	70p			74LS332	240p	74S387	80p	4556	36p
7493A	85p			74LS333	240p	74S388A	80p	4557	240p
7494	110p			74LS334	240p	74S389A	80p	4558	140p
7495A	80p			74LS338	240p	74S374	75p	4008	80p
7496	80p			74LS340	240p	74S375	75p	4008	80p
7497	210p			74LS342	80p	74S377	130p	4009	45p
74100	80p			74LS343	80p	74S378	130p	4010	45p
74107	80p			74LS347	80p	74S379	130p	4011	24p
74109	75p			74LS348	80p	74S381	450p	4012	25p
74110	75p			74LS349	100p	74S385	325p	4013	36p
74111	65p			74LS351	240p	74S390	80p	4014	60p
74116	170p			74LS354	240p	74S393	100p	4015	70p
74118	110p			74LS355	240p	74S396A	100p	4018	35p
74119	170p			74LS373A	30p	74S399	140p	4017	55p
74120	100p			74LS374A	35p	74LS445	100p	4018	80p
74121	85p			74LS375	45p	74LS465	120p	4019	90p
74122	70p			74LS376A	30p	74LS487	120p	4020	80p
74123	60p			74LS383A	70p	74LS490	150p	4021	80p
74125	65p			74LS385	75p	74LS540	100p	4022	70p
74126	65p			74LS386	75p	74LS541	100p	4023	30p
74128	55p			74LS390	40p	74LS508	70p	4024	48p
74132	75p			74LS391	80p	74LS510	100p	4025	24p
74136	70p			74LS392	55p	74LS512	100p	4026	24p
74141	80p			74LS393	80p	74LS522	100p	4027	40p
74142	280p			74LS395B	75p	74LS526	225p	4028	40p
74143	270p			74LS396	80p	74LS528	225p	4029	75p
74144	270p			74LS107	40p	74LS529	125p	4030	36p
74145	110p			74LS109	40p	74LS540	200p	4031	125p
74147	170p			74LS112	45p	74LS540-1		4032	100p
74148	140p			74LS113	45p			4033	125p
74150	175p			74LS114	45p	74LS641	150p	4034	130p
74151A	70p			74LS122	70p	74LS642-1	80p	4035	200p
74153	90p			74LS123	80p			4036	70p
74155	140p			74LS124	80p	74LS643	250p	4037	110p
74158	100p			74LS125	80p	74LS644	300p	4038	100p
74157	80p			74LS126	80p	74LS645	300p	4039	250p
74159	175p			74LS132	85p	74LS645-1	200p	4040	100p
74160	110p			74LS133	80p			4041	225p
74161	80p			74LS136	45p			4043	225p
74162	110p			74LS138	55p	74LS668	80p	4044	280p
74163	110p			74LS139	55p	74LS669	80p	4045	100p
74164	120p			74LS145	85p	74LS670	170p	4046	100p
74165	110p			74LS147	175p	74LS682	250p	4047	120p
74166	140p			74LS148	140p	74LS684	350p	4048	120p
74170	400p			74LS151	65p	74LS687	350p	4049	100p
74170	200p			74LS152	200p	74LS688	350p	4050	100p
74172	420p			74LS153	80p	74LS783	521	4051	85p
74173	140p			74LS154	150p			4052	150p
74174	110p			74LS155	65p	74S SERIES		4053	180p
74175	105p			74LS156	65p	74S00	80p	4054	180p
74176	100p			74LS157	65p	74S02	50p	4055	180p
74178	150p			74LS158	65p	74S04	80p	4056	85p
74179	150p			74LS160A	75p	74S06	80p	4059	80p
74180	150p			74LS161A	75p	74S06	80p	4080	75p

### LINEAR ICs

AD7581	£18	LM3094C	400p	TBA231	180p
AD7581	1180p	LM709	70p	TBA280	180p
AM79100C	£25	LM710	100p	TBA280	180p
AM103	300p	LM711	100p	TBA280	180p
AV-1-5050	180p	LM723	75p	TBA280M	

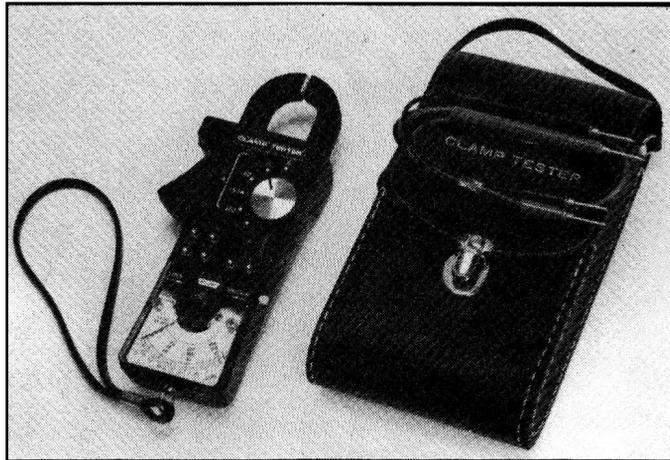
● West Hyde claims to be the leading supplier of cases and accessories to the UK electronics industry. The company's Spring 1987 catalogue contains 104 A4 pages and lists both metal and plastic enclosures suitable for just about every imaginable application. Case accessories such as handles, knobs, feet and ventilation grilles are included and there are also sections devoted to switches, indicators, tools and component storage systems. West Hyde Developments Ltd, 9-10 Park Street Industrial Estate, Aylesbury, Buckinghamshire HP20 1ET. Tel (0296) 20441.

● GP Electronic Services has acquired a small number of the Symot cassette mechanisms specified for use in last month's Telfax project. The mechanisms are designed for use with endless tape cassettes as explained in the text and GP is offering them for an all-inclusive price of £15 while stocks last. Contact GP Electronic Services, 87 Willowtree Avenue, Durham DH1 1DZ.

● From somewhere or other Greenweld Electronics has managed to acquire a stock of the defunct Enterprise 64 computer. There are several hundred of them, all brand new and boxed, and they are being offered at an all-inclusive price of £3995. For that you get a Z80-based machine with 64K of RAM, 256 colours and on-board word processor. Greenweld Electronics Ltd, 443 Millbrook Road, Southampton SO1 0HX. Tel (0703) 772 501.

● IC Electronics offers a wide range of products by mail-order including components, tools, electrical appliances, records and games. The company's latest catalogue includes an extensive selection of telephones and accessories plus watches, clocks, calculators, car loudspeakers, tape players and many more items. Copies cost 60p (refunded on first order) from IC Electronics Business Centre, PO Box 130, Aberdeen AB9 8QH.

● Sage Audio has developed a dual-rail power supply module which is said to offer the smoothest regulated DC output on the market. It is designed for use in pre-amplifiers and offers 200mA at either  $\pm 12V$ ,  $\pm 15V$ ,  $\pm 18V$  or  $\pm 36V$ . Sage claims the output noise and ripple level is 1000 times less than obtained from 78/79 series IC regulators and that the unit also offers improved line and load regulation. Prices start at £20 inclusive. Sage Audio, Construction House, Whitley Street, Bingley, West Yorkshire BD16 4JH. Tel (0274) 568 647.



## Low-Cost AC Clamp Tester

**C**lare Instruments has introduced a clamp tester which is claimed to be the cheapest available in the UK.

It measures DC resistance as well as AC voltage and current and costs £32 plus VAT.

Like other clamp testers, the Clare ST 300 uses a current transformer to measure the AC current flowing in a conductor. This removes the need to break into a circuit to make current measurements, simplifying the test procedure and greatly reducing the risks where mains voltages are involved.

In use, the jaws of the tester are simply clamped around the current-carrying conductor. Cables of up to 28mm overall diameter can be accommodated and the current is displayed in five ranges with FSDs from 6A to 300A.

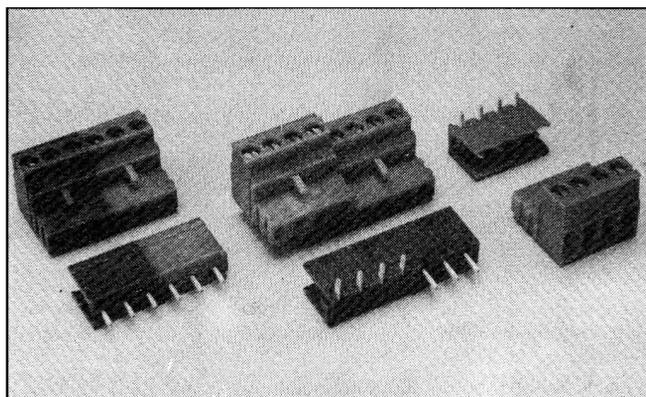
AC voltage is measured using

a set of plug-in test leads and displayed in three ranges, from 150 to 600V FSD. The fuse-protected resistance range also uses the plug-in leads and has an FSD of 1k $\Omega$  and a centre-scale value of 30 $\Omega$ . Accuracy is  $\pm 3\%$  of FSD for voltage and current and  $\pm 3\%$  of reading for resistance.

A useful feature is the scale lock which clamps the meter needle in position when operated. This allows readings to be taken in poor light or in awkward positions and the reading preserved for subsequent checking.

The Clare ST 300 measures 196 x 86 x 46mm and comes complete with test leads and 1.5V AA battery in a sturdy carrying case.

Clare Instruments Ltd, Woodsway, Goring-by-Sea, Worthing, West Sussex BN12 4QY. Tel (0903) 502 551.



## Many Ways To A Good Connection

**P**rinted circuit board connectors can be made up to any number of ways and colour-coded for identification using a new modular terminal system from Components & Electronics Ltd.

The board-mounting plugs and matching cable sockets are available with two, three or four ways and will slot together to form longer connectors. The plugs have straight or right-angled pins for soldering to a PCB while the

sockets are equipped with screw terminals.

A positive latching action prevents accidental disengagement of mated connectors and a series of ridges on one side only provides polarisation. All sizes are available in both red and green versions to allow colour-coding of connector assemblies.

Components and Electronics Ltd, PO Box 88, Haslemere, Surrey GU27 2RF. Tel (0428) 54141.

## The Shrinking Compact Disc

Philips and Sony have announced joint plans to develop several new consumer electronics products based on compact disc technology.

With the standard compact disc already well established as an alternative to 12 inch analogue LP's, the two companies have decided to develop a smaller CD which will be able to compete effectively with 7 inch 'single' records.

Single music tracks are already available on standard-sized CDs but reducing the playing time in this way doesn't bring the production costs down. Existing CD singles are therefore comparatively expensive.

No standard has been agreed for the new CD single but the initial proposal is that it will be a 3" disc capable of carrying up to 20 minutes of music. New compact disc players would handle both sizes of CD while a simple adapter would enable the 3 inch disc to be played on existing equipment.

The two companies are also planning to develop a standard sized compact disc which will carry five minutes of combined music and video. This would complement the larger, longer playing video discs already in use and would prove an ideal medium for pop videos.

The music and video disc would be coloured gold to distinguish it from music-only CDs and the audio track would be replayable on standard compact disc players.

In time, it is anticipated that companies will develop combination optical disc players providing both audio and video outputs of high quality. These would handle all the different sizes of disc now in use or under development.

## Amstrad Gets BBC Apology

The BBC has apologised unreservedly after receiving a libel writ from Amstrad.

The action followed the publication of an article in Ariel, the BBC's house magazine, which questioned the safety of Amstrad's PC1512 IBM clone.

Amstrad admits there have been several enquiries about the absence of a mains lead on the 1512 but insists that none is needed. The machine has full BEAB class II certification and can be operated safely without an earth.

Amstrad has accepted the apology and says it will not be pursuing the libel action.

## Putting On A Colourful Face

**M**ulti-colour front panels with a professional finish can be produced quickly and easily using a new process devised by Mega Electronics.

The Gedakop system uses thin aluminium sheets which are pre-coated with a light-sensitive photoresist. A positive artwork carrying the required panel markings is laid over the aluminium sheet which is then exposed in a light box.

The board is developed with water to leave a positive image of the artwork which will accept colour dyes. The dyes will not attach to the non-image area and any excess or unwanted dye can be removed with a stripping solution.

When complete, the aluminium can be sealed to protect the coloured image against scratching and chemical damage.

Mega supply the pre-coated aluminium in a range of sizes from 250 x 230mm up to 500 x 1000mm and in thicknesses from 0.125 to 3.0mm. Twenty-nine different dyes are available and they can be mixed to produce an almost infinite range of colours.

An introductory kit consisting of two pre-coated sheets, black dye and stripping solution costs £16 and further dyes can be obtained for £4.50 each. There is also a comprehensive starter kit costing £43 which includes four 160 x 250mm sheets of aluminium in various thicknesses, four different colour dyes, thinner, touch-up solution, stripper and various accessories. These prices do not include VAT, and there is a £2 post and packing charge on all orders.

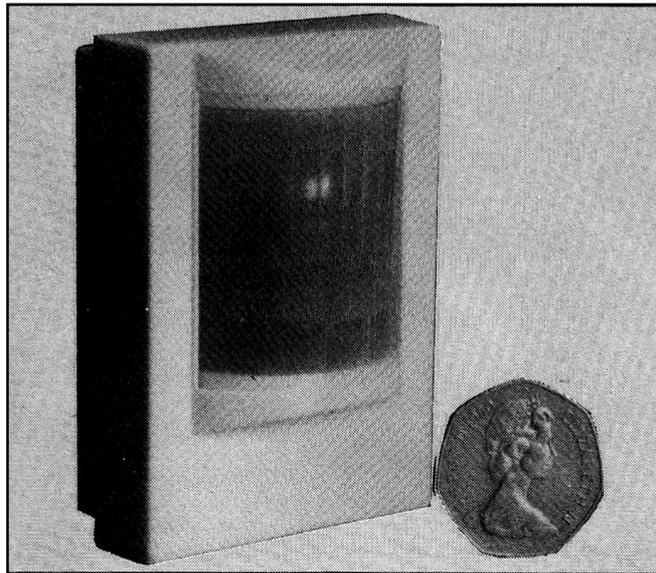
Mega Electronics Ltd, 9 Radwinter Road, Saffron Walden, Essex CB11 3HU. Tel (0799) 21918.

## More Jobs In Electronics

41% of employers in the electronics manufacturing industry plan to take on more staff during the second quarter of 1987 according to a survey conducted by temporary staff specialist Manpower PLC.

This is slightly higher than the figure for the same period last year (39%) and well up on the 27% recorded during the first quarter of 1987.

The number of employers planning to cut jobs has risen slightly from 11% last quarter to 12% for the next quarter, but this figure is still an improvement on the 15% figure obtained for the same period last year.



## Miniature Infra-Red Detector

**R**iscomp has introduced a passive infra-red detector suitable for use in many automation and security applications.

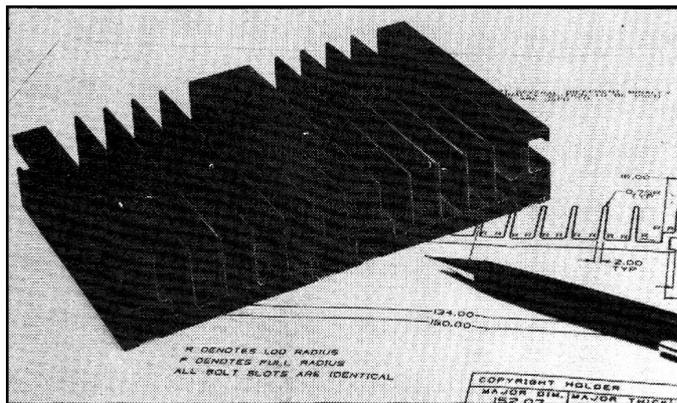
It senses body heat at distances up to 12 metres in an 85° arc and responds by closing a relay. The output could be used to switch on a porch light or an alarm or even to operate an automatic door or other entry control system.

The RP33 detector uses a 24-facet Fresnel lens to give graduated coverage in three vertical planes. This allows the detector to be at its least sensitive

near the ground where movements from animals might cause false alarms.

The RP33 is designed for easy installation and its small size (80 x 60 x 40mm) allows it to be hidden in almost any recess. A switchable walk-test facility allows the effective range to be checked during setting-up. Operation is from a 12V supply and full installation instructions are provided.

The RP33 costs £23.95 and is available from Riscomp Ltd, 51 Poppy Road, Princes Risborough, Buckinghamshire HP17 9DB. Tel (08444) 6326.



## Boxing Clever With Heatsinks

**A** new range of heatsinks from Marston-Palmer has an unusual interlocking feature which allows several heatsinks to be connected together to form box structures or large panels.

Known as the Comb-Lok range, the new heatsinks have two lipped grooves on each side, positioned at right angles to each other. When the groove on one extrusion is lined up next to the groove on another, an X-shaped coupling extrusion can be slid into place to lock the heatsinks together. The grooves will also accept caged nuts so that

heatsinks can be attached to a panel without being drilled.

Comb-Lok heatsinks are available in ten standard extrusion profiles from 75 x 25mm up to 300 x 40mm and in a range of lengths from 75 to 250mm. Thermal efficiencies range from 3.4°C/W for a 100mm length of 75 x 25mm extrusion down to 0.5°C/W for a 100mm length of 300 x 40mm extrusion.

Marston-Palmer Ltd, Wobaston Road, Fordhouses, Wolverhampton WV10 6QJ. Tel (0902) 783 361.

The latest Rapid Electronics catalogue runs to 128 A4 pages and includes a number of new product lines. Cases and test equipment are among the ranges which have been expanded along with tools, PCB drafting aids and etching kits. Copies are available free-of-charge from Rapid Electronics, Hill Farm Industrial Estate, Boxted, Colchester, Essex CY4 5RD. Tel (0206) 272 730.

● Free from Analog Devices is an 8-page booklet called 'Analogue-to-Digital conversion Using Voltage-to-Frequency Converters'. It describes several methods of using a V-F converter in an ADC system and includes notes and circuit diagrams for a 16-bit converter and several other configurations. Copies are available from Analog Devices, Central Avenue, East Moseley, Surrey KT8 0SN. Tel 01-941 0466.

If owning a dog sounds a bit too much like hard work (all those 'walkies' and trying to read copies of ETI with teeth marks) you may prefer to build TK Electronics' microchip mongrel. Better known as kit XK125, it is designed to deter burglars and simulates the sound of any dog from a terrier to an alsatian. The XK125 kit is not included (as far as we can see) in the otherwise quite comprehensive TK catalogue, but a whole range of other products are, including semiconductors, cases, test equipment and all the usual stuff. Plus, of course, kits. TK Electronics, 13 Boston Road, London W7 3SJ. Tel 01-567 8910.

● Law enforcement agencies in America are using a high resolution scanning system to speed up the processing and retrieval of fingerprints. Instead of using a conventional ink and paper approach, suspects' finger prints are scanned electronically and then digitized for storage. The resulting data can be found instantly from among a vast number of other prints, can be compared electronically in a computer with other prints to aid identification and can be sent down the telephone line to other police stations and centres. The system is expected to speed up the processing of suspects.

● Believe it or not, you can now buy calculators and watches which are said to be water-powered. All they need is to be immersed in water every few months and they will go on working for ages. It all seems too good to be true. If anyone can explain how this works we'd be happy to hear from them. Meanwhile we're trying to obtain a few samples for review.

NEXT MONTH

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INTERNATIONAL

## KAPPELLMEISTERS

Vot do you sink you are doingk listening to zose deredful loudshpeckers. Built a pair of ETI's Kapellmeister transmission line units immediately or suffer ze consequences ov der horrid hi-fi for ze rest of your life.

## SURFACE MOUNTING

As commercial electronic equipment gets smaller and smaller ET/ takes a look at the surface mounting process while it's still visible.

## TELEPHONE ALARM

In these days of high technology there's no need to disturb the neighbours with a lot of bells and sirens when you're being burgled in your absence. Fit an ETI Telephone Alarm and keep in touch.

## AND IN THE BLUE CORNER

Everything you always wanted in an electronics mag but were afraid to even hope for. News, diary, Tech Tips, practical projects, fascinating features, readers' ads, and much, much more. Don't miss it.

# Don't miss the July issue of ETI

# - out 5th June

All the articles listed are in an advanced state of preparation but circumstances beyond our control may prevent publication.

## Zenith Electronics

### Kits - Modules - Hardware

YOU KNOW US FOR OUR TRANSMITTER KITS - NOW TAKE A LOOK AT OUR GROWING RANGE OF QUALITY KITS AND READY-BUILT PROJECTS. MODULES AND ELECTRONIC HARDWARE

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- ★ 3 Note Electronic Door Chime unit; 9 volt operation, 3 melodious tones; variable frequency. Kit £9.83.
- ★ 300 Watt Light Dimmer unit for 240 volt mains lights. Kit £6.95
- ★ 5 Code Digital Code unit plus Key Pad—select own code; 9 volt. Kit £14.21.
- ★ 5-100 Watt Electronic Loudspeaker Overload Protector, adjustable. Kit £11.11.
- ★ VU Meter 10 LED indicator; -5 to +12dB range. Kit £12.59.
- ★ Automatic light controller; automatically turns on and off lights at pre-set times and triggered by darkness. Kit £25.08.
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- ★ Amplifier Power Meter; 10 LED indicator from 0.25-100 Watt Input—9 volt operation. Kit £9.52.
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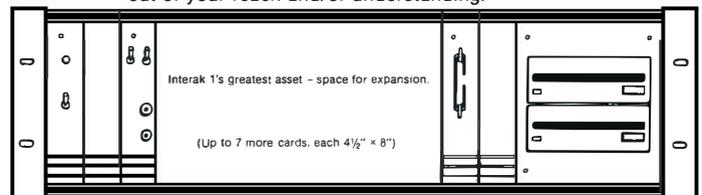
Zenith Electronics, 14 Cortlandt Business Centre,  
Hailsham, E. Sussex, U.K. BN27 1AE.  
Tel: 0323 847973 Dept 2.

## Interak 1

### AN EXPANDABLE DISK-BASED Z80A DEVELOPMENT SYSTEM YOU CAN BUILD YOURSELF!

Universities, Colleges, Industry, Enthusiasts:

Unlike home computers, development systems have entirely "open" architectures, use standard TTL etc. chips (ie no ULA's!), and are built in a proper engineering fashion. Usually these superior products carry a correspondingly superior price tag, but you can build Interak yourself board by board and thus afford a system which would normally be out of your reach and/or understanding.



Z80A CPU | 64K DRAM | 64 x 24 VDU | YOUR OWN EXPANSION (EG. SPEECH, SOUND, EPROM, PRINTER, MODEM, TAPE, RELAY, CONTROL, INTERFACING, ETC. ETC.) | ASCII KEY BOARD | DISK INTER FACE | 2 x 1 MBYTE 3 1/2" DISKS (EXAMPLE)

The initial development system has 64K of RAM, a 4 MHz Z80A CPU, parallel ASCII keyboard interface, VDU interface (TV set or monitor), and a floppy disk drive interface for up to 4 drives. Any size (including 8" double density) can be used, but our 1 Megabyte 3.5" drives are proving very popular because they can fit into the system rack, (and they only cost £94.00 each + VAT). CP/M Plus is available, giving access to thousands of "public domain" programs.

The system can be described as "future proof" because it uses plug in 4.5" x 8" cards in an industrial quality 19" 3U rack. We have been established since 1970, and this system was first made in 1977 so (unlike almost all other computers) it has stood the test of time.

Send two second class stamps, or telephone for a detailed descriptive leaflet, specification, prices, etc.

## Greenbank

Greenbank Electronics (Dept T6E), 460 New Chester Road,  
Rock Ferry, Birkenhead Merseyside L42 2AE. Tel: 051-645 3391

## British Electronics Week — April 28-30th

Olympia Exhibition Centre, London. See February '87 ETI or contact the Evan Steadman Communications Group on (0799) 26699.

## Digital Audio Tape Recording — April 30th

The IEE, London. See March '87 ETI or contact the IEE at the address below.

## Tool Kits And Sneaky Tricks — May 15th

The IEE, London, 2.00pm. Discussion meeting. Contact the IEE at the address below.

## TV Displays: The Next Ten Years — May 20th

The IEE, London, 2.00pm. Discussion meeting. Contact the IEE at the address below.

## Computer North — May 27-29th

G-Mex Complex, Manchester. Business computer show. Contact Cahners on 01-891 5051.

## UK Telecommunications Networks: Present & Future — June 2-3rd

IEE, London. Conference. Contact the IEE at the address below.

## CableSat '87 — June 2-4th

Metropole Hotel, Brighton. Exhibition and conference. Contact Online at the address below.

## International ISDN Conference — June 15-18th

London. Conference on the Integrated Services Digital Network. Contact Online at the address below.

## Networks '87 — June 16-18th

London. For details contact Online at the address below.

## Condition Monitoring For Safety — June 25th

Regent Crest Hotel, London. Seminar and Exhibition. Contact ERA Technology on (0372) 374 151.

## Satellite Communication Systems — July 26-31st

University of Surrey. Vacation school organised by the IEE. Contact them at the address below.

## Designing For Electromagnetic Compatibility — September 13-18th

University of Sussex. Vacation school organised by the IEE. See address below.

## Design Engineering Show — September 15-18th

NEC, Birmingham. Exhibition and conference covering all areas of engineering including electronics and CAD/CAM. Contact Cahners on 01-891 5051.

## IDEX '87 — September 21-23rd

Metropole Exhibition Halls, Brighton. See April '87 ETI or contact Nutwood Exhibitions on (04848) 25891.

## Automotive Electronics — October 12-15th

The IEE, London. International conference organised by the IEE in conjunction with many other professional bodies. Contact them at the address below.

## Radar '87 — October 19-21st

Kensington & Chelsea Town Hall, London. International conference on civil and military systems organised by the IEE and the American IEEE. Contact the IEE at the address below.

## International Video & Communications Exhibitions — October 18-21st

Metropole Exhibition Centre, Brighton. Exhibition with seminar programme covering video equipment, services, programme production, etc. Contact Peter Peregrinus Ltd at the IEE address below.

## Electronic Displays — November 17-19th

Kensington Exhibition Centre, London. Contact Network Events at the address below.

## Interact '87 — November 17-19th

Kensington Exhibition Centre, London. Exhibition and conference covering all aspects of interactive technology including touch screen displays, interactive videos, computer training systems, etc. Contact Network Events at the address below.

## Addresses:

Institution of Electrical Engineers, Savoy Place, London WC2 0BL. Tel 01-240 1871.

Online Conferences Ltd, Pinner Green House, Ash Hill Drive, Pinner, Middlesex HA5 2AE. Tel 01-868 4466.

Network Events Ltd, Printers Mews, Market Hill, Buckingham MK18 1JX. Tel (0280) 815 226.

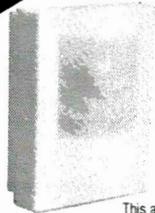
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## 500W Quartz Halogen Floodlight FL 500



**only £14.95 + VAT**

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Consisting of separate transmitter and receiver both of which are housed in attractive moulded cases, the system provides an invisible modulated beam over distances of up to 50ft operating a relay when the beam is broken. Intended for use in security systems, but also ideal for photographic and measurement applications. Size 80 x 50 x 35mm

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# HART

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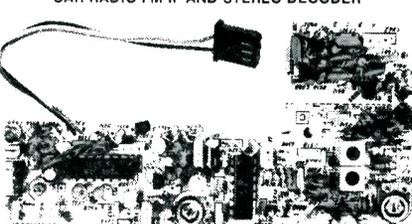
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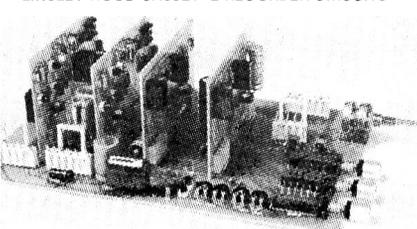
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## LINSLEY-HOOD SYNCHRODYNE AM RECEIVER

Very high quality kit for this recent design featured in 'Wireless World'. This unit represents the first attempt to make a much needed HIGH QUALITY AM Tuner since pre-FM days. This will give you Radio 4, or even 1 in better quality than your Eastern 'Tranny'. Advanced construction system, approved by the Author, uses 3 double sided PCBs in a stacked layout for total stability, ease of construction and minimal wiring. This module will form the AM section of an ultra high quality AM/FM switched bandwidth tuner to match our 300 series amplifiers. Power supply and tuning gang will be included **£59.95**

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Do your tapes lack treble? A worn head could be the problem. Fitting one of our replacement heads could restore performance to better than new! Standard mountings make fitting easy and our TC1 Test Cassette helps you set the azimuth spot-on. We are the actual importers which means you get the benefit of lower prices for prime parts. Compare us with other suppliers and see! The following is a list of our most popular heads, all are suitable for use on Dolby machines and are ex-stock.

**HC20 Permalloy Stereo Head.** This is the standard head fitted as original equipment on most decks ..... **£7.86**  
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Please consult our list for technical data on these and other Special Purpose Heads. **MA481 Latest version Double Mono (2/2) Record/Play head.** ..... **£13.35**  
Replaces R484 ..... **£13.35**  
**SM166 Standard Mounting 2/2 Erase head.** Compatible with above or HQ551 4-Track Head ..... **£8.85**  
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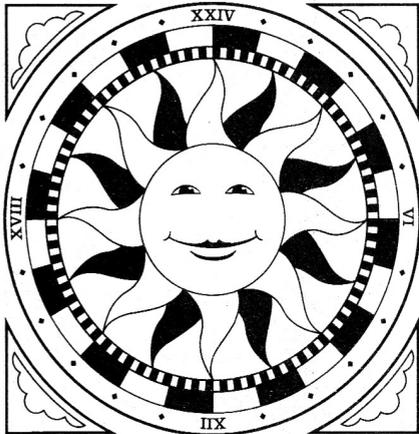
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# READ/WRITE



## Gno Hope

I am sorry to have to report an unfortunate deficiency in your normally exemplary standards of technical nomenclature.

I am referring, of course, to the central, raised part in your 24 Hour Sundial project. Surely it was unnecessary to introduce the ugly neologism 'shadow caster' for a component which has been known for centuries (as anyone with pretensions to a proper education would tell you) by the generally accepted term 'gnomon'.

I have more sympathy with your nameless colleague, though, who in suggesting the helicopter variation obviously had in mind a new meaning for 'tempus fugit'.

Terry Richter  
Fareham, Hants.

**We had gno idea our readers were so knowledgable in the art of sundial construction. Gnext time we shall gnow better.**

Anyway, 'Gnomon' is really meant to describe a shadow caster (there's that awful phrase again) formed like a leant-over L shape. The ETI Sundial uses a much more elegant swept curve. (That's our excuse and we're gnot going to budge!).

## Hoodwinked

You asked for it. The world is going to pieces (Read/Write March 1987). You could help prevent it by insisting John Linsley Hood presents an up-to-date cassette deck project

With the design of analogue recording circuitry about to become an arcane art, it behoves you to see that everyone has at least a chance of building (not to mention understanding) a cassette deck of the quality with which J LH is normally associated.

I have built a number of his designs, including the ETI 100W MOSFET amp. I doubt I am alone in according totally with him when he claims it to be the best he has yet heard.

Please, then: a cassette deck which can be connected to such an instrument without fear of committing heresy.

Ivor Colwill  
Haywards Heath, Sussex.

**Give the man a chance. J LH is already working on an updated MOSFET amp and a new integrated amp for us. Not to mention a couple of other projects too. We promise that as soon as he has finished that little lot we'll try to persuade him of the joys of a truly hi-fi cassette deck. Meanwhile, have patience and make do with current heretical models.**

## The Right Rate

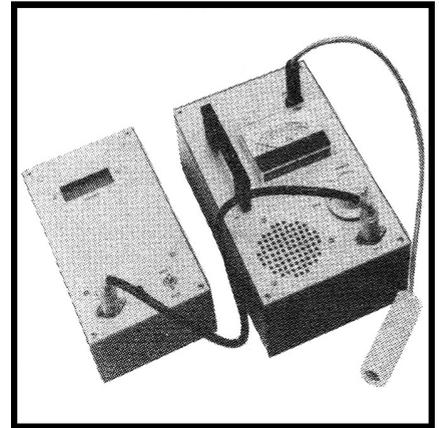
Referring to your article 'Geiger Ratemeter and Counter' in the February and March 1987 issues of ETI, I think readers should be warned that testing foodstuffs for contamination is not as simple as suggested.

It is not just a matter of applying the probe to, say, a joint of meat and, because there is no count rate increase, assuming all is well. The meat tissues could still be dangerously contaminated with alpha particles which are not detected because they can travel only a very short distance through tissues (less than 1mm).

The official method of testing a carcass is to burn it to ashes and test the ashes with a wide area gas flow type monitor.

Alexander Turner  
Richmond, Surrey.

**Thanks for the information. The ETI Geiger meter project will still find (accurate) uses for many readers in other types of radiation testing.**



## Virtuous Virtuoso

I read with interest the letter from D.W. McDonald in the April issue concerning his desire for a complete set of audio equipment in kit form from John Linsley Hood. His ideas echo plans formulated by Audiokits over the last 15 months.

In a short period we have introduced two preamps, a power amp and an integrated amplifier all of which can be built in standard or 'upgraded' versions. Since ETI published our Virtuoso preamp last year we have received many calls and letters from delighted customers all over the world.

The cases we supply are to the same quality as those we supply to specialist hi-fi shops.

I can assure Mr. McDonald that Audiokits is doing the things he is seeking and has many other exciting developments in the pipeline.

Graham Nalty, Audiokits  
Borrowash, Derby.

**ETI hopes to publish the Virtuoso Power Amplifier to accompany last year's preamp and also from Graham Nalty, in the near future.**

*ETI is pleased to receive your letters on any topic—past, present or future. If you want to know something or think we should be told of something, don't hesitate, write in to the ever-open arms of the ETI post room. Write to:*

**Electronics Today International  
1 Golden Square  
London W1R 3AB**

# THE TELEPHONE SYSTEM

You may not believe it but the UK telephone system is the best in the world. Keith Brindley explains why.

There are two main different switching methods used in wired telecommunications systems. The type used in all analogue public switched telephone systems is called 'circuit switching'. A transmission circuit or channel is set up between the caller and whoever is being called by switching together whatever individual transmission links are required in the system to form the channel. The channel remains set up throughout the call and only ends when one or both users hang up.

For interest the other main type of switching method is message switching. Here each block of communication is sent over the system individually, making its own way from caller to receiver via whatever transmission links are necessary.

Every new block makes its own way and so it is conceivable that many different transmission paths will be used to make up the whole communication. No single channel exists between the two users. A derivative of message switched telecommunications systems is British Telecom's 'Packet Switch Stream' (PSS) used for digital computer data communications.

Large circuit switched systems like the Public Switched Telephone Network (PSTN) must be hierarchical in nature. That is, switching centres (usually called exchanges) must exist at different levels in the system so that a user at one point in the system can call another user by linking together whatever exchanges are necessary to form the circuit.

Figure 1 shows the layout of a hierarchical telephone system where exchanges are layered to allow any two telephones in the system to communicate. The bracketed term after each exchange type is the commonly used name in the UK system. Larger telephone systems, such as the North American system, may use a further layer of exchanges above tertiary exchanges (quaternary trunk exchanges).

Although a hierarchical system with so many interconnections between different levels of exchanges may seem unnecessary, there is a reason why PSTNs are so constructed. If an exchange between two users is busy (fully utilised with no spare lines) as a call is set up, the call is easily redirected around that exchange and on to another.

Being busy is not the only reason why an exchange is unusable, of course, it may be faulty. Alternative routing ensures the PSTN we've considered still keeps working overall. I would venture to suggest this is the very reason why British Telecom's PSTN kept working during the recent BT telephone engineers' strike. It wasn't that faults weren't occurring. It was just that the system is so well designed as to keep working even with the faults.

In terms of numbers, there are something like 21 million or so local lines in the British PSTN and something over 6000 local exchanges. Of the local exchanges, about half are electromechanical 'Strowger' exchanges (you know: click, click, whirr, whirr, clatter, clatter, clatter!). About 2000 are reed relay exchanges which, although electromechanical, are at least

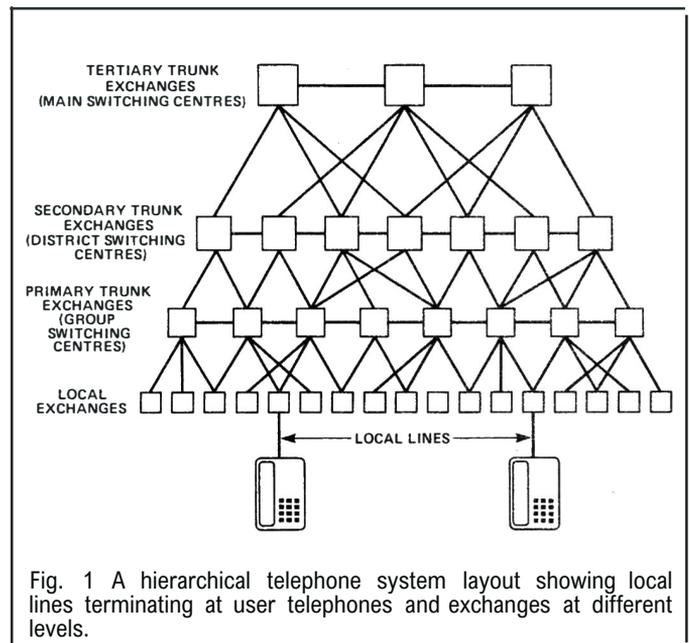


Fig. 1 A hierarchical telephone system layout showing local lines terminating at user telephones and exchanges at different levels.

computer-controlled. About 500 are crossbar electromechanical exchanges and (wait for it) *only about 500* are digital exchanges (and I said this is the best system in the world?).

## X Rated

Of the digital exchanges about 150 are small rural exchanges while the remainder (only about 350) are so-called System X exchanges.

System X exchanges are now being commissioned at the rate of about one per week. That sounds pretty impressive until you work out at that rate it will take about 5500 weeks (105 years) to convert the rest of the system! Nevertheless, it's hoped to get rid of all Strowger local exchanges, replacing them with computer-controlled reed relay types at the very least, by 1992. Target for a completely digital PSTN (this includes user's telephones, as well as exchanges) is the year 2014.

In the trunk network, things are proceeding much faster. Of the 55 digital exchanges planned 54 have already been commissioned, so BT's target of a fully digital trunk network by 1988 should easily be met. Finally, to get out of the British PSTN, four digital international trunk exchanges are planned, of which two have been commissioned.

## Traffic control

Now it's possible the average reader doesn't think much of the British PSTN! Nevertheless, an awful lot of thought and planning goes into the system which isn't immediately apparent. Even if you do reckon that too many calls don't get through, it's a fact that the actual

probability of call failure due to blocking is very low. If you *do* have serious problems making calls it just may be that your problems lie in your telephone unit, or in your own fingers.

The main aim of any PSTN is to provide an acceptable telephone system at an acceptable price. Obviously, users want a system which works and which doesn't cost the earth. Any PSTN provider must therefore ensure sufficient amounts of exchange equipment are available to keep the probability of call blocking low enough for acceptability — without providing so much equipment that the service is too expensive.

We've used the term probability pretty loosely but it can be (and is) used in its strict mathematical sense to help calculate the amount of equipment required to provide an acceptable yet economic telephone system. If the system is considered as a number of distinctly separate parts as in Fig. 2 then the overall probability of a call being blocked between one user and another is given by:

$$P = 1 - ((1 - P_1) (1 - P_2) (1 - P_3) \dots (1 - P_n))$$

where  $n$  is the total number of parts used in the call and  $P_1, P_2$ , etc are the probabilities of calls blocking at each part of the system over which the call is routed. If the probabilities of blocking are very small (which hopefully they are) then this expression simplifies to:

$$P = P_1 + P_2 + P_3 + \dots + P_n$$

This means the overall probability of a call being blocked can be directly broken down into the probabilities of each separate piece of equipment used in the call routing.

Simple enough, but we still need to relate the probabilities of call blockages to the numbers of calls which the system must cater for. Calculating the amount of calls made in a PSTN is an important aspect in planning the system and the usual method of doing it measures telephone usage in terms of *traffic* — the average number of calls over a given period of time.

A Danish mathematician, Agner Erlang, did a significant amount of work in calculating telephone traffic, and his name is used as a dimensionless unit of traffic. So, an average of 100 concurrent calls is known as 100 erlangs of traffic.

If, say,  $n$  calls are made during a period of  $T$  seconds, and the durations of the calls are  $h_1, h_2, h_3, \dots, h_n$  seconds then the use of the system is:

$$\sum_{i=1}^{i=n} h_i \quad (\text{call-seconds})$$

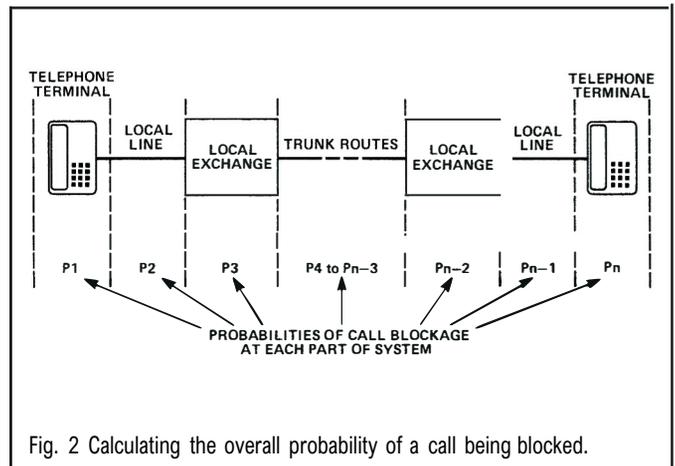
The traffic (the amount of calls per unit time) is thus:

$$E = \frac{\sum_{i=1}^{i=n} h_i}{T} \quad (\text{erlang})$$

From this we can calculate what is known as the mean holding time (the average call length) given by:

$$h = \frac{\sum_{i=1}^{i=n} h_i}{n} \quad (\text{seconds})$$

If we refer to the average rate at which new calls appear as a calls per second, then a much more useful



expression for traffic is given by:

$$E = ah \quad (\text{erlangs})$$

Now we can relate traffic with blocking probabilities to calculate the exchange equipment required to maintain an acceptable service. If there are  $K$  calls in progress and  $N$  pieces of exchange equipment each of which can handle one call then the probability of calls blocking is given by:

$$P = \frac{E^N / N!}{\sum_{k=0}^{k=n} E^k / k!}$$

which means that we can now calculate the number of pieces of exchange equipment to maintain any desired probability, knowing the traffic which the exchange has to handle.

Fortunately, it's not necessary to work with these expressions every time an exchange is being planned or updated. Once the ideal numbers have been calculated for any desired probability, straightforward look-up tables may be constructed which relate the two. Table 1 gives examples of the numbers of pieces of exchange equipment required to maintain a probability of call blockage of less than 0.01 for a number of different values of traffic.

## Terminals and Local Lines

Local lines within the PSTN (lines between the users' premises and the local exchange) are twisted pairs. The

Traffic (in erlangs)	Pieces of exchange equipment
0.1	2
0.5	4
1.0	5
5.0	11
10.0	18
50.0	63
100.0	117

Table 1 Number of pieces of exchange equipment required to maintain a probability of call blocking less than 0.01 for various levels of traffic.

characteristics of any pair of wires carrying analogue signals are determined by the constants of capacitance, resistance, inductance, and conductance. Further the transmission properties can be represented by a wire pair's characteristic impedance and propagation constant. All constants are related by the complex mathematical expressions:

$$Z_0 = ((R + j\omega L) / (G + j\omega C))^{1/2}$$

$$\gamma = ((R + j\omega L)(G + j\omega C))^{1/2}$$

where:  $Z_0$  = the characteristic impedance,  $R$  = the resistance per unit length,  $\omega$  = the angular frequency of the applied signal,  $L$  = the inductance per unit length,  $G$  = the conductance between the two wires per unit length,  $C$  = capacitance between the two wires per unit length, and  $\gamma$  = the propagation constant.

These expressions allow us to define the various constants of the wires for any particular frequency. Local lines, with only a few exceptions, use audio frequencies and so their transmission properties are fairly well classified although variations do exist.

Local lines comprise a single twisted pair. This means that incoming and outgoing speech signals are imposed on the same line. At the exchange and at the user's telephone these signals must be separated. If no separation occurred at the telephone, the signal produced by the handset microphone would be fed to the earphone in a process known as 'sidetone'.

However, a small amount of sidetone is desirable, so the user does not feel the system is 'dead'. Figure 3 shows the basis of a typical circuit used in telephones to separate the two directions of signals on the local line while maintaining some sidetone. While some modern telephones use more complicated versions, this shows in principle how signals are split and combined.

## In the end

As far as the user is concerned, local lines are terminated inside the user's premises, at a network termination point usually called a 'master' socket. At present, plugging into the master socket is the closest a user may officially get to the local line but it's just possible that this situation may change in the future. For now, it's the network provider's responsibility (that is, British Telecom for the national PSTN, Mercury Communications in the case of its telephone network and the Kingston-upon-Hull Telephone Department in the Hull telephone network) to terminate the local line. However, from 1st of December last year, extension socket wiring may be undertaken by people (including users) other than the network providers.

It's important to note, though, that any extension wiring undertaken by non-network providers *cannot be hard-wired into the master socket*. It can only be plugged in! Figure 4 shows this diagrammatically. It is, in fact, illegal to tamper with a master socket, or extension sockets wired by the service provider, in any way except by plugging in to them.

This means that a user who does not yet have a master socket fitted and who wants to plug in an extension circuit, first must ask the network provider to fit a master

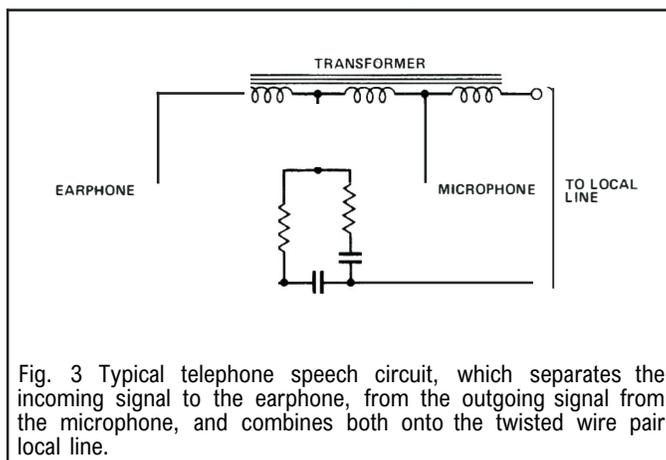


Fig. 3 Typical telephone speech circuit, which separates the incoming signal to the earphone, from the outgoing signal from the microphone, and combines both onto the twisted wire pair local line.

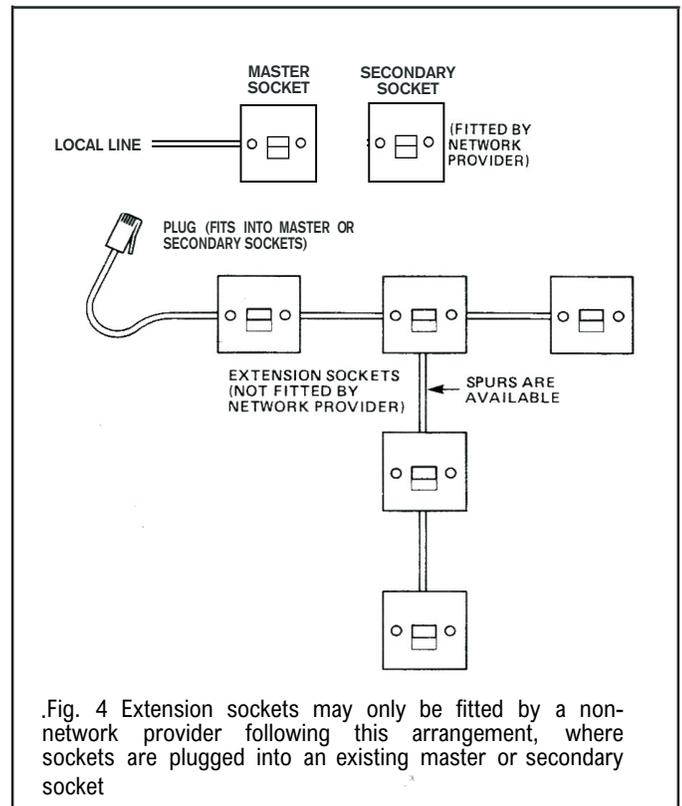


Fig. 4 Extension sockets may only be fitted by a non-network provider following this arrangement, where sockets are plugged into an existing master or secondary socket

socket — at a fee (BT currently charges £10 & VAT, plus a visit charge of £15 + VAT if no other chargeable work is carried out at the time of conversion).

## Toeing The Party Line

Incidentally, if a user has a party line (a line shared with another user) sockets cannot be fitted to the line. This does not mean the user with a party line can't have sockets. The network provider is under an obligation to provide them. In such a case it is up to the network provider to replace the party line with a standard non-party local line and fit the sockets.

So, if you have been forced to have a party line, and you don't want one, simply ask for sockets to be fitted. It'll cost you the £25 + VAT conversion charge but it's one way of getting your own back on BT. There's nothing BT can do to make you keep the party line!

Master sockets and extension (technically known as 'secondary') sockets are identical in outward appearance and contain a printed circuit board onto which the socket itself is fastened. Master and extension sockets, in fact, usually contain the same circuit board, but extensions do not have all the components present in the master. Figure 5 shows the basic circuit of the master socket, how the socket is connected to the twisted pair local line and how the network provider will hard-wire connections to any extension which it provides.

Capacitor C1 is known as the 'bell' capacitor. Before the era of sockets this was housed in each telephone. It provides the simple function of isolating the bell inside any telephone connected to the master or extension sockets from the local line, as far as DC is concerned. For the majority of the time the bell is effectively unconnected. When a call is placed to a user and the bell is to ring, the local exchange transmits an AC signal which is passed by the bell capacitor and so rings the bell.

Resistor R1 is known as the 'out-of-service' resistor. This has two main functions. First, if a call is placed, the out-of-service resistor maintains a circuit even if all telephones are unplugged. To the user trying to call, the ringing tone is still heard. Second, if a user is in

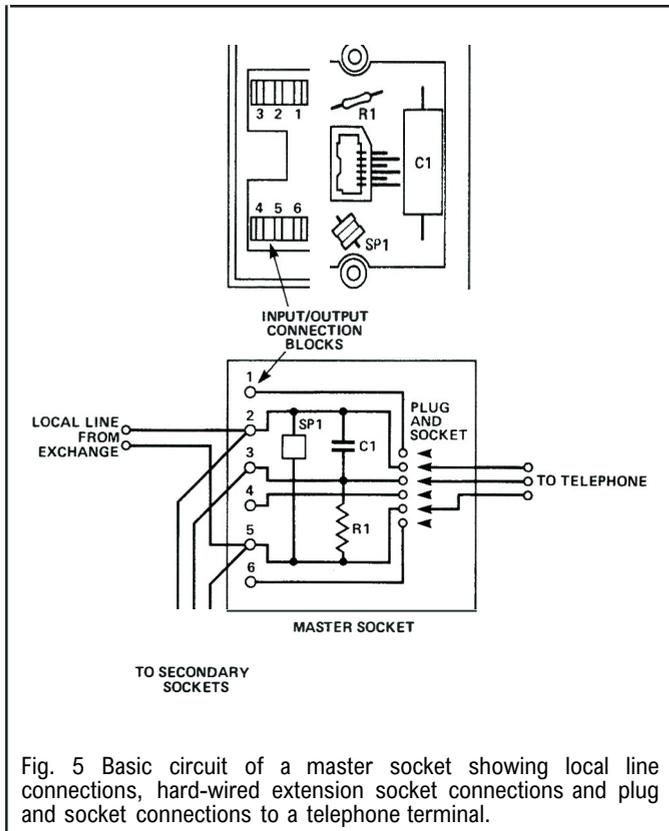


Fig. 5 Basic circuit of a master socket showing local line connections, hard-wired extension socket connections and plug and socket connections to a telephone terminal.

communication with another user but wishes to take the call in another room, the telephone may be unplugged and taken to another socket. The out-of-service resistor maintains the circuit and thus holds the line open until the telephone is plugged in again.

Component SP1 is a 'surge arrester' to prevent incoming high voltage peaks on the line from getting to the telephone and outgoing high voltage peaks getting onto the line.

## Tinkle, Tinkle, Little Star

Having the bell capacitor present in the master socket gives a number of benefits.

The main one is that extension telephones to be used are merely connected in parallel (via extension sockets). If you did this on a local line terminated without the master socket, all telephones would 'tinkle' when one

telephone is dialing out.

The master socket's internal bell capacitor allows a third 'anti-tinkling' connection to be made to each telephone. When one telephone is to be used to dial out, it short-circuits the bell capacitor and tinkling simply cannot occur. A further benefit is that the capacitor is not now needed inside the telephone — helping to reduce telephone cost.

All sockets have six connections, although only three of these are used in standard telephone wiring. You may wish to use the others in baby alarm or intercom type applications, but to do this you'll need to wire extensions with six-core cabling, instead of the standard four-core cabling usually used. Table 2 relates the colour coding of the wires of the cable to the socket connection numbers.

Although it doesn't particularly concern us here, it's interesting to note that above local exchange level in the PSTN hierarchy, single twisted pairs aren't used for transmission. Instead, a four-wire link is used (two wires for one direction of signal, two wires for the other direction) all in a twisted form (twisting is used to minimise interference). Above this in the hierarchy, trunk routes use multiplexed signals (multiplexed in either frequency or time) on four-wire links, coaxial cables, optical fibres, or sometimes microwave radio links.

## Dialing out

Having considered the local line and the termination points at the user's premises, it's only right we now look at the signals which are transmitted *along* a local line to and from the master socket. The majority of telephone terminals (the actual devices you make and take calls with) in use in the British PSTN are presently known as loop disconnect signal terminals. This refers to the dialing method the phones use.

Figure 6 shows a typical terminal connected via a local line to the local exchange, together with basic internal circuits within the exchange. The master socket is also shown with its internal bell capacitor.

Although the device used to dial a number is shown as an old-fashioned rotary dial, most modern phone terminals use a push-button dial which provides exactly the same function: the dial breaks the circuit once for every value of each digit dialed. So, if the digit five is dialed, the circuit is broken five times. If digit two is dialed the circuit is broken twice. Slightly misleadingly, if digit zero is dialed, the circuit is broken ten times.

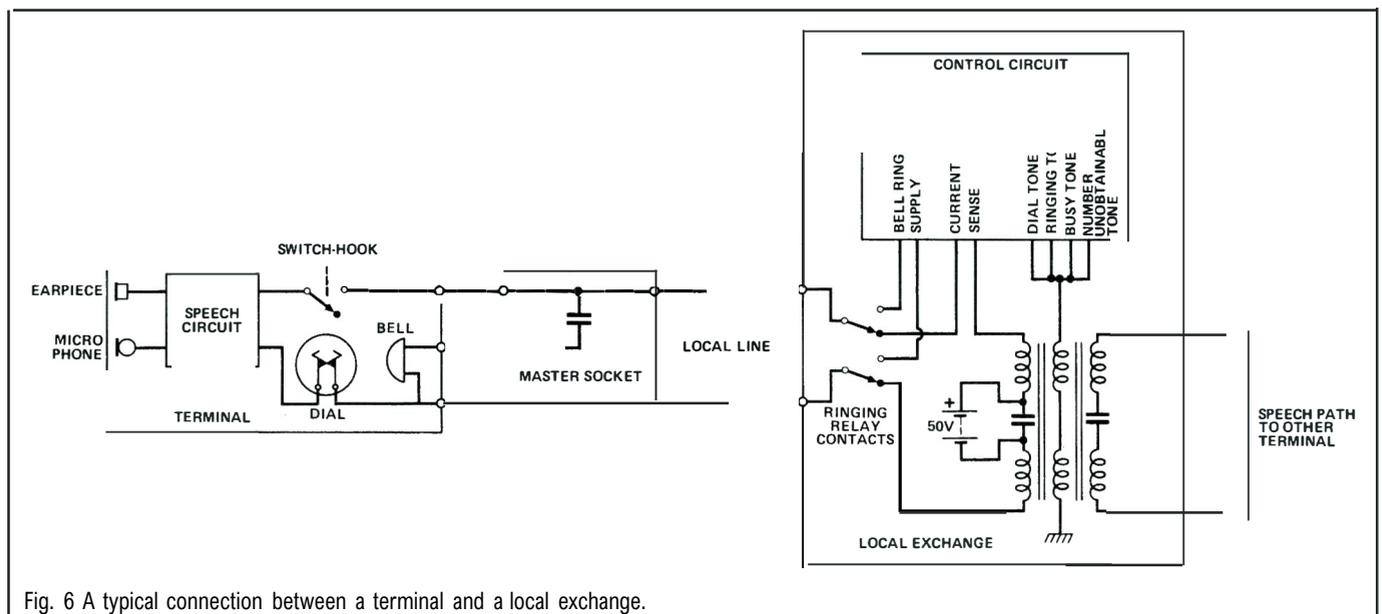


Fig. 6 A typical connection between a terminal and a local exchange.

That's why the name 'loop-disconnect signal' is used for this method of dialling.

The circuit is also broken when the telephone handset is replaced on the switch-hook and that's where we'll start the description of operation. With the handset on the switch-hook the circuit is broken and no direct current can flow from the local exchange. As soon as the handset is lifted the circuit is closed, and the speech circuit of the terminal is connected across the local line.

The speech circuit has a fairly low resistance (in the order of 100 ohms) and so direct current flows in the local line via the 50 volt DC power source and speech transformer T1. The current is sensed by the control circuit and is interpreted as a 'call-request' signal. In response to the call-request, the control circuit injects a tone supply corresponding to the dialling tone through the central coil of transformer T1. The tone is thus inserted onto the local line, resulting in the same tone being heard in the earphone at the user's phone terminal.

On hearing the dialling tone the user starts to make the call, dialling the number required digit by digit. The control circuit senses each time the circuit is broken during a digit and counts the breaks to calculate which digit has been dialled. The period of these breaks is not usually too critical — somewhere around 10 breaks per second (normally called 10 pulses per second, or 10pps) is typical. The length of time *between* breaks is important. If, say, a time of greater than about 200ms occurs, the control circuit is able to sense what is interpreted as an 'inter-digit pause' — the circuit senses that one digit has ended and the next is about to start.

When the call is routed through to the receiving telephone terminal, a ringing tone is obtained from the receiving terminal's local exchange. It's interesting to note, though, that the ringing tone is produced, as we'll see soon, by the other user's local exchange and not by the user's phone being rung. So, just because you can hear a ringing tone, it doesn't mean the other phone is actually ringing! There may be a fault between the other user's local exchange and that terminal or the terminal may be unplugged from its socket.

Two other tones may be sent to the calling terminal from the control circuit. Number unobtainable or busy tones may be sent if either of these conditions occur when the call is made.

Socket connection	Wire colour (principal colour first)
1	green/white
2	blue/white
3	orange/white
4	white/orange
5	white/blue
6	white/green

Table 2 Telephone wire colour coding with reference to telephone socket terminal connections.

## It's For You-hoo

The local exchange also has a great deal to do with signals going to a telephone terminal. When a terminal is to be called, for example, the control circuit at the local exchange first senses if current is flowing in the local line. If it is, then the terminal is in use. That is, the terminal is busy and the call cannot proceed. If not, then the control circuit can ring the terminal's bell by operating a relay whose contacts break the local line from the speech transformer and instead connect them to a bell ringing supply. The bell ringing supply is of an interrupted AC form at a frequency of 17Hz and of 75 volts. The AC ringing signal is passed by the bell capacitor in the user's master socket, causing the terminal bell to ring.

The control circuit senses the bell ringing (if current is flowing, the bell is assumed to be ringing) and injects a ringing tone onto the speech path via the central coil of transformer T1. This informs the user making the call that the called terminal is ringing. As soon as the terminal handset is lifted, however, the control circuit senses the call has been answered and de-energises the ringing relay, re-connecting the local line to the transformer, and so completes the speech channel between the two telephone terminals.

## Them Tones, Them Tones...

Although loop-disconnect signalling is currently the most common form of digit signalling in the British PSTN, this is only because most local-exchanges are of Strowger or similar electromechanical types. Newer digital exchanges can cope with other forms of signalling, one being 'dual-tone multi-frequency signalling' (DTMF, for short). DTMF phones are push-button but unlike loop-disconnect types of push-button phones they don't break the circuit to indicate digits. Instead a combination of two tones is transmitted down the local line from the terminal to the local exchange for each digit pressed. The tones are detected at the local exchange and the digit is consequently calculated.

Figure 7 shows the tones standardised by the CCITT for DTMF signalling. Each row and each column of the set of push buttons is allocated a particular tone so that when a button is pressed, the tones corresponding to the row and the column the button is part of, is transmitted down the line.

DTMF signalling allows a considerable increase in the speed with which a call can be set up. In the loop-disconnect system pulses are transmitted at about 10pps, so a typical telephone number of seven digits can take anywhere between about 700ms and 8.4s to transmit between terminal and local exchange. In the two extremes, the number could be any between the shortest possible (1111111), and the longest possible (0000000). Also, the inter-digit pause, typically 200 ms, has to be added to every digit dialled.

Different numbers dialled by the DTMF method, on the other hand, do not affect the time taken for signal transmission. Instead, the time depends largely on the speed with which the user can push the buttons!

## Hanging On The Line

There are five basic categories of equipment of interest to the house telephone user which can be plugged into a telephone socket. Any equipment must be approved by the British Approvals Board for Telecommunications (BABT) and must comply with certain standards and regulations.

To show that equipment is approved and complies with all standards and regulations, any device will carry a 'green circle' approval sticker or label. If no 'green circle' is present, it is illegal to plug the device into your telephone sockets, so beware. The five categories of equipment which can be used on the PSTN are:

- Simple extension telephones. Ordinary, basic phones with no extra features.
- Telephones with loudspeaker, monitor, or modem facilities. The type of phone with simple VDU characteristics used for connecting to viewdata services, etc.
- Cordless telephones.
- Telephone answering/recording machines.
- Modems, or non-speech equipment which incorporates a modem.

The important British Standards which relate to all equipment connected to telephone lines are BS6301, BS6305, and BS6317. Any equipment containing a modem

must also comply with BS6320. Any equipment requiring a mains power supply must also comply with BS6484. The plugs used to connect the equipment to a telephone socket must themselves comply with BS6312. These standards are by no means exhaustive but provide a starting point for approvals purposes.

## Onwards, Ever Onwards

Recently, unless you lived in the Kingston-upon-Hull district, you could only have a telephone through British Telecom. Since liberalisation — choices have begun to appear. Cellular telephones, for example, provide a means whereby mobile telephone communications independent of BT can be obtained.

Of greatest significance in the long run is the telephone network provided by Mercury Communications. Still in its infancy now, this network will rapidly become a national PSTN service and a real alternative to BT's PSTN.

Initially, at least, home users will be able to connect to the Mercury network via existing local lines and a special Mercury network when making a call. A rental for the BT-owned local line will be due, however, whether or not users actually make calls via the BT PSTN.

The Mercury network itself is digital, so offers greater quality than BT's network. But linking via existing local lines to the Mercury network limits quality to that of the BT analogue local line. Eventually, BT's own network and local lines will be digital and Mercury may offer its own local lines to customers. Whatever happens improved services are on the way.

The problems of waiting for a digital service do not occur for certain users. Existing business telephone users may already be able to access the Mercury network

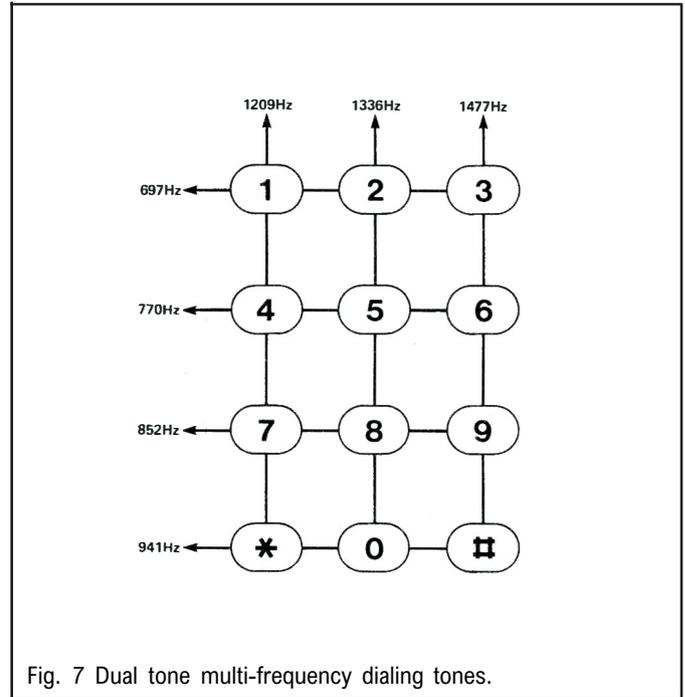


Fig. 7 Dual tone multi-frequency dialing tones.

directly, via cable, fibre optic, or microwave link. Likewise BT can link business users directly into its digital trunk network. So high quality digital telephone communications are already possible.

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# HARDWARE

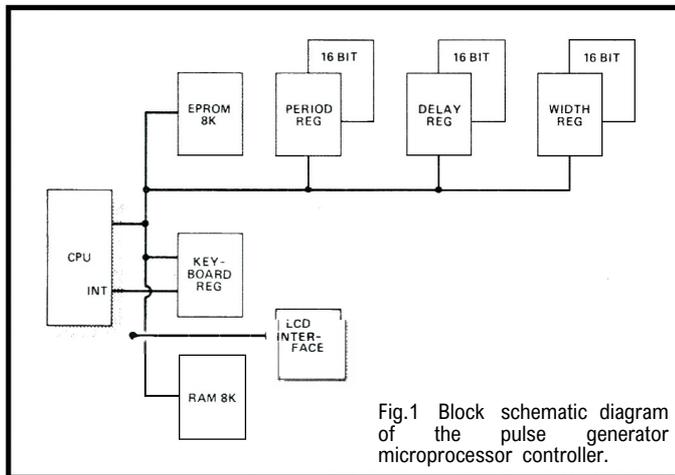
# DESIGN CONCEPTS

## FEATURE

Mike Barwise polishes off the design of his pulse generator with a look at the control board and an algorithm to run the whole system.

Now that we have designed the pulse generator itself, the time has come to consider how to program and control it. A simple solution is to use a conventional eight bit microprocessor addressing a bank of storage registers attached to the programming bus of the generator boards.

There is also a need for some kind of convenient user input and display, so that the required information can be passed to the pulse generator in a *convenient* manner. The general circuit schematic is shown in Fig. 1.



### Automating Parameter Settings

The simplest pulse generator with only one range has no settability problem. There is only one possible setting of the control registers for a given output. Remembering that each generator stage adds a clock cycle to its time on top of the set modulo and that each following stage takes a clock cycle to respond to its predecessor's start request, we simply arrange to subtract three from the entered parameter for Delay and one from those for Period and Width to provide perfect settability.

The pulse generator which switches range on Period Delay and Width simultaneously (in other words, with all three parameters always set to the same range) has a slight settability problem. If, as in our design of pulse generator, the adjustment ratio (1:4095) exceeds the range spread (1:10), there are already several alternative setting parameters which could yield the same output (where the ranges overlap).

One solution to automation is always to pick the settings which require the fastest possible range, thus maximising setting *resolution*. Aside from this, the same calculations apply as to the single range system.

However, we have given ourselves a somewhat greater problem by allowing the Period, Delay and Width to be independently range switched. The additional cycles detailed earlier still have to be added to the timing chain

but the question now is how long is each additional cycle.

Once the period, delay and width are set to different ranges, each has a clock cycle of different duration. We must therefore identify the relevant clock for each additional cycle and add *time* rather than *cycles* to our parameter definition.

In practice, the same approach of going for the fastest range possible is still probably the best as it maximises setting resolution. However, the assessment must now be made for each element individually rather than globally for the system.

An outcome of this which may not be immediately apparent is that what you ask for may not be exactly what you get. The pulse generator may be forced to choose the nearest setting to your selection if it is not able to accomplish the absolute setting.

This should be considered when designing the user input and display handling. Should you ignore discrepancies, thereby providing inaccurate results but boosting user confidence, or do you report setting discrepancies, yielding high reliability but resulting in a less 'user friendly' system?

### Direct Control

The third alternative is for all parameters to be directly controlled by the user from the keyboard. This is the most flexible and precise method but demands such a high level of user awareness of the pulse generator mechanism that it is not really practicable. No one but the designer would be able to use the system!

To sum up then, we will be automatically selecting the fastest range possible for each parameter (Period, Delay, Width) and will display (although this is just my preference) the actual parameters used by the system. This means that what you enter at the keyboard and what you get at the output and on the front panel display will sometimes be a little different but the discrepancy is both predictable and documented.

The general algorithm for input to actual conversion is as follows and is shown in Fig. 2.

Starting with pulse width, choose a range, then program the width registers with one less than the required modulo to allow for the stage characteristic. Establish the delay range and modulo, then subtract one from the modulo for the stage characteristic and one for the start cycle. The result is the modulo to be programmed into the delay register. Remember that the real delay will be greater by *one width range* clock period, due to the Width start cycle.

Finally, establish the Period range and modulo and subtract one cycle for the stage characteristic.

The only parameter which will be subject to discrepancies will therefore be the Delay. Note though that even when the zero Delay option is in use, the start cycle will still cause a minimal delay.

# FEATURE

The user display should reflect these small discrepancies, so the user will know what is *actually* happening. The discrepancies will in fact be very small in most cases.

The worst case is when working at the fastest end of three adjacent ranges, such as Width 200 nanoseconds, Delay 2 microseconds, Period 20 microseconds where the delay may depart from ideal by up to 10%. It will, however, be totally stable, precise and repeatable. The same discrepancy will always be present.

This amounts to a limitation on 'settability', rather than precision, and should prove quite acceptable in practice.

## Implementation

There are many alternative approaches to the microprocessor control. I have selected my own favourite devices although I'm sure that other people will prefer different solutions and can convincingly argue for them. This is a good area for experimentation as the microprocessor setup is comparatively slow and simple.

I chose my old faithful favourite, the 6502 (the 1MHz version is all you really need here), using a hardware scanned keyboard and a Densitron intelligent LCD display module (available from RS and, of course, Electromail) as user input and output devices.

The keyboard circuit is shown in Fig. 3. A binary counter drives an active low output decoder (least significant two bits) and an eight-to-one multiplexer (most significant three bits).

The decoder outputs form the rows of the key matrix and the multiplexer inputs (pulled high) form the columns. Pressing a key connects a decoder output to a multiplexer input and when the counter gets round to the mutual selection point of the connected input and output, the multiplexer output goes low.

This signal is used to stop the counter and the current count is then passed to a CPU mapped register. A delayed interrupt generator allows for switch bounce before flagging the CPU to read the key code.

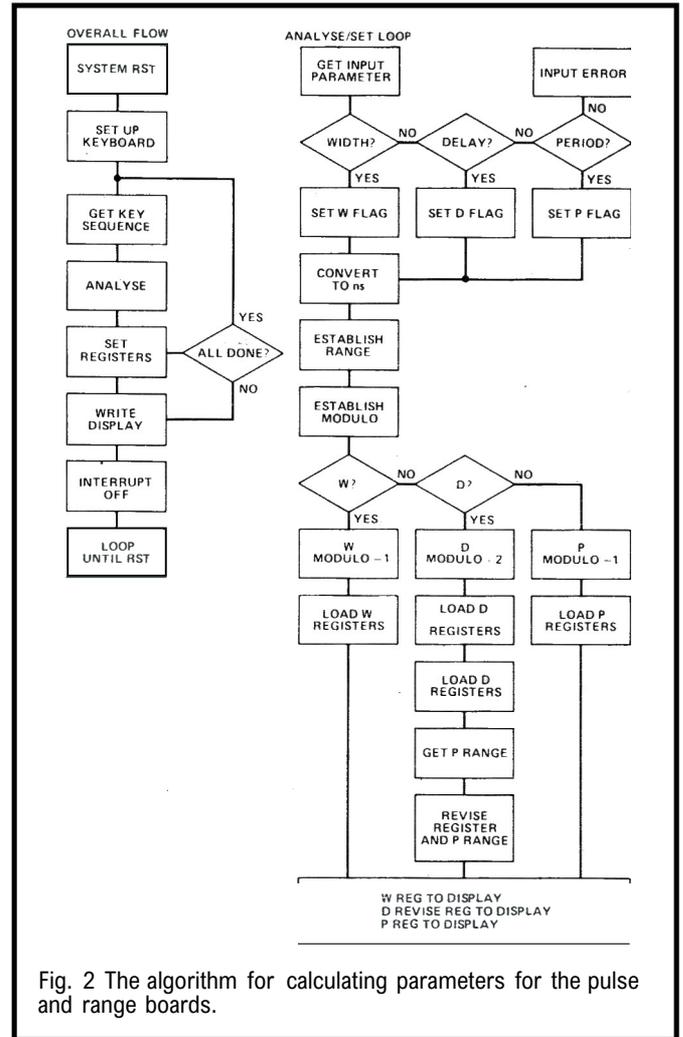


Fig. 2 The algorithm for calculating parameters for the pulse and range boards.

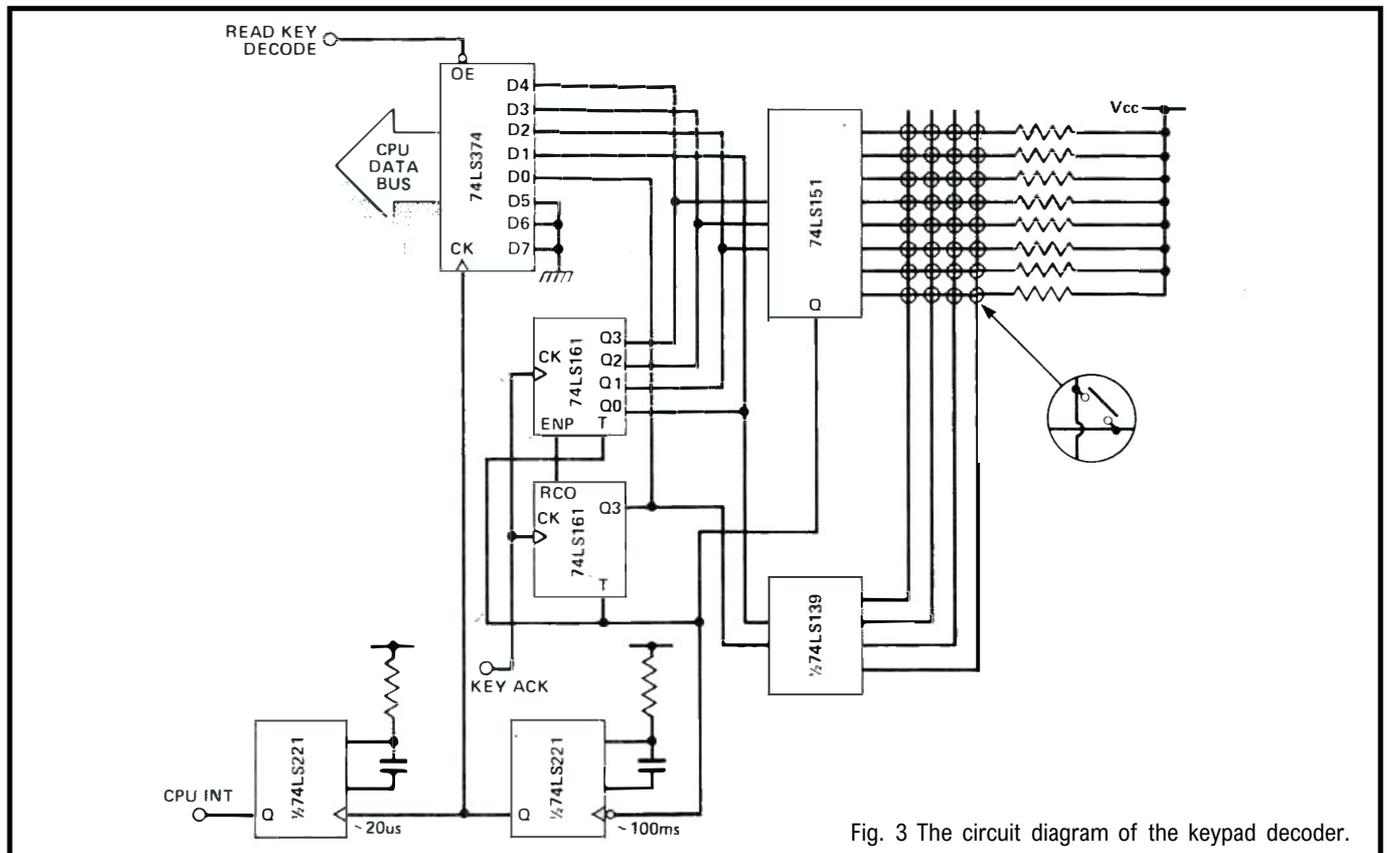


Fig. 3 The circuit diagram of the keypad decoder.

Each time the switch bounces, the counter will rescan the matrix and stop at the same key code as before. If the stop signal were simply piped through to the CPU interrupt, although the key code would be valid, it would be read an arbitrary number of times.

The answer is to delay the generation of the interrupt until the key has stopped bouncing. The simplest way to do this is to use a pair of non-retriggerable monostables. The first closure of the key starts the first monostable which then ignores further triggers until it has timed out. If its time period is in the order of 100ms, the key can be guaranteed closed and stable before the period ends.

The trailing edge of the first monostable pulse clocks the counter data into the keyboard interface data register and also starts the second monostable, which generates the CPU interrupt.

No attempt has been made to convert the keyboard output to ASCII. We only need about 20 keys and so the key code can be used as an entry to a ROM based lookup table.

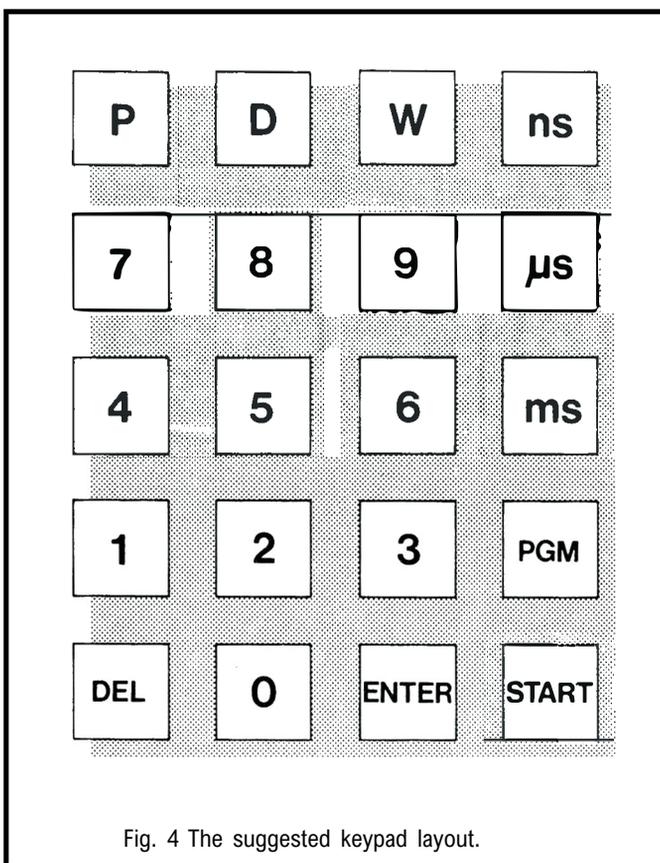


Fig. 4 The suggested keypad layout.

The recommended keys are: **0-9** plus **Delete** and **Enter** for decimal input, **nS**, **uS**, **mS** for input scaling, **P**, **D**, **W**, for period, delay and width and finally **PGM** to halt the generator for reprogramming and **Start** for restarting after programming. The suggested keypad layout is shown in Fig. 4.

The PGM key is not on the scanned matrix. It is in fact the CPU reset button. This is because it is a good idea to turn off the CPU interrupts (thus disabling the keyboard) while the pulse generator is running. Reset is then used to attract the attention of the CPU for reprogramming. The CPU is in fact just idling at all times except while programming.

## Display

The display driver is the simplest possible solution. The Densitron display requires an eight bit data byte and a strobe while data is valid (rather like a Centronics

printer interface on a microcomputer). There are, however, two internal registers — data and command. As we are only interested in seven bit data (ASCII alpha-numerics), I have used the eighth bit as the register select.

This means that commands are sent as straight ASCII and data for display are negated with (bit 7 set). This limits the display versatility a little, but greatly simplifies the interface.

Referring to Fig. 5, data bit 7 (MSB) is grounded at the display, and the display Read/Write pin is strapped to Write. Data 0-6 are supplied from a latch together with the RS (register select) which replaces D7 of the incoming data byte.

Timings are fairly critical as these displays are quite slow. Note the use of a transparent latch (74LS373) rather than an edge triggered register for data storage. This allows us to meet the long data setup time required by the display and still generate the enable strobe directly from the register write signal.

The only remaining unfamiliar element is the pot across pin 3. This is a bias voltage to adjust the display contrast. Anything in the 10K region is about right but a padder resistor could be needed at the top end. For more detail on this and for the actual programming codes, I refer you to the manufacturer's data sheet.

The final point to mention about the display is that it is most easily read from just *below* its normal axis, so clever mounting may be needed.

This more or less wraps up the pulse generator design. I have been less specific about the control end of the unit as I feel this is much more likely to be familiar to you. The real aim has been to guide you through the design process, rather than just run a pulse generator project, but I hope some of you give it a go and build one. It's back to pure concepts next month with a thorough investigation of programmable logic.

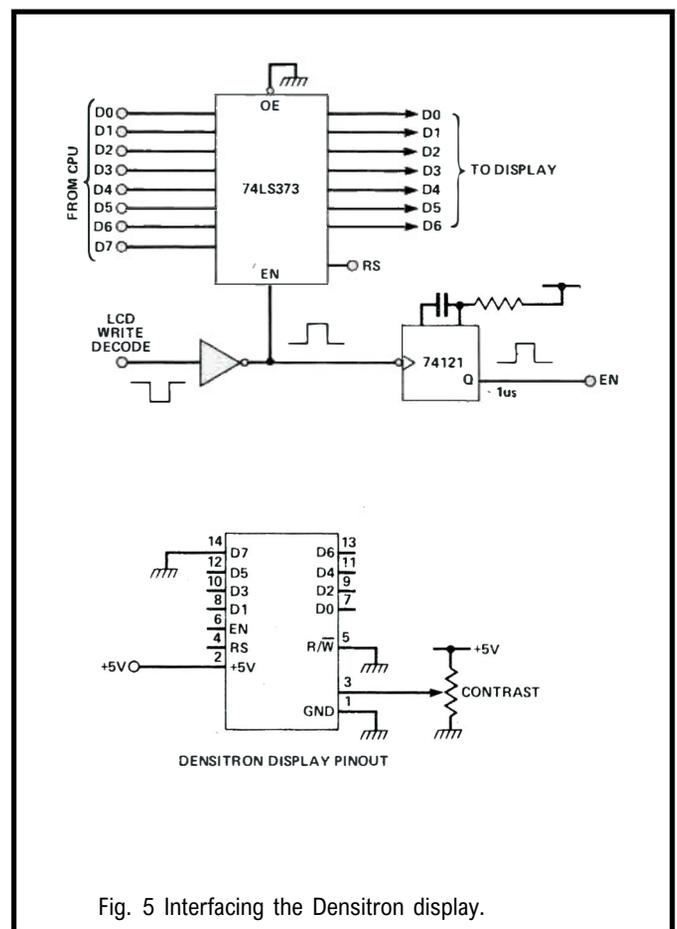


Fig. 5 Interfacing the Densitron display.

# CIRCUIT THEORY

Paul Chappell gets into some pretty heavy mathematics to explain the workings of the Fourier series.

The Fourier series is no more mysterious or complicated than the Taylor or Maclaurin series expansions which you will remember from your school days. Instead of expressing a function as an infinite polynomial, it is expanded into a series of sine waves.

Figure 1 shows how this works with a square wave. The building begins with a sine wave of the same frequency as the square wave we are trying to make. At point A a smaller sine wave at three times the frequency is added, at point B yet another sine wave at five times the frequency of the original is added.

With each addition the rise becomes steeper, the top becomes flatter and the resulting waveform becomes closer and closer to a square wave. The process continues with addition of 7th harmonic, then 9th, and so on.

The Fourier series has the form:

$$f(x) = a_0 + \sum_{n=1}^{\infty} (a_n \cos(nx) + b_n \sin(nx))$$

At the moment this doesn't express any kind of mathematical truth. It's really more like a wish. We hope that, given a function  $f(x)$  we can choose values for the coefficients ( $a_n$  and  $b_n$ ) to make the two sides of the equation identical, in which case we will have found the Fourier series for  $f(x)$ .

Whether this can be done for any function or just for some we don't yet know. There clearly are functions for which the expansion *does* hold because we can take the process the opposite way around. If coefficients are selected at random and  $f(x)$  is made equal to the result, then  $f(x)$  is its own Fourier expansion! (There's no need to choose an infinite number of coefficients. As soon as you get bored, the rest can be set to zero!)

Take another look at the form of the Fourier series. If the summation sign is alien to you, it's just a shorthand way of saying:

$$f(x) = a_0 + a_1 \cos(x) + b_1 \sin(x) + a_2 \cos(2x) + b_2 \sin(2x) + \dots$$

Since all the sines and cosines vary about zero, the  $a_0$  is needed to represent the mean level (the DC component if we're thinking about voltages). The reason for having both sines *and* cosines is to give the relative phase of the various components. For instance, adding equal quantities of  $\sin(x)$  and  $\cos(x)$  will give a wave  $45^\circ$  out of phase with each.

To find the values of the coefficients it is convenient to make use of a property of sines and cosines known as orthogonality.

## Orthogonality

This is the name for a special disappearing trick that sines and cosines perform. If you draw a graph of  $\sin(x)$  over the interval 0 to  $2\pi$  (one complete cycle), I think you'll agree that the area above the axis exactly matches the area below. So, if you integrate between these limits, the two areas 'cancel out' and leave you with zero, right? Exactly the same thing applies to a cosine, over the same interval.

Draw a graph of  $\sin(2x)$  over the interval 0 to  $2\pi$  (two complete cycles) and the area above matches the area

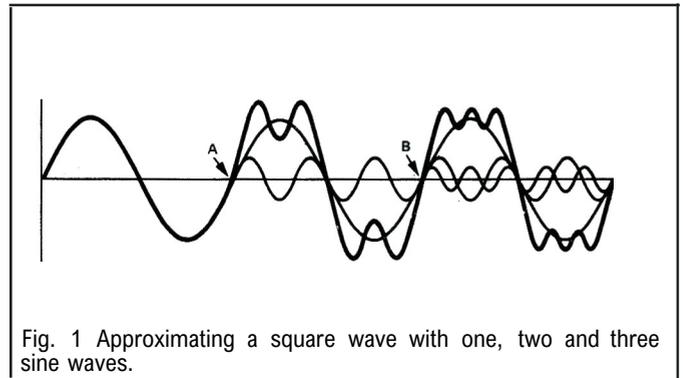


Fig. 1 Approximating a square wave with one, two and three sine waves.

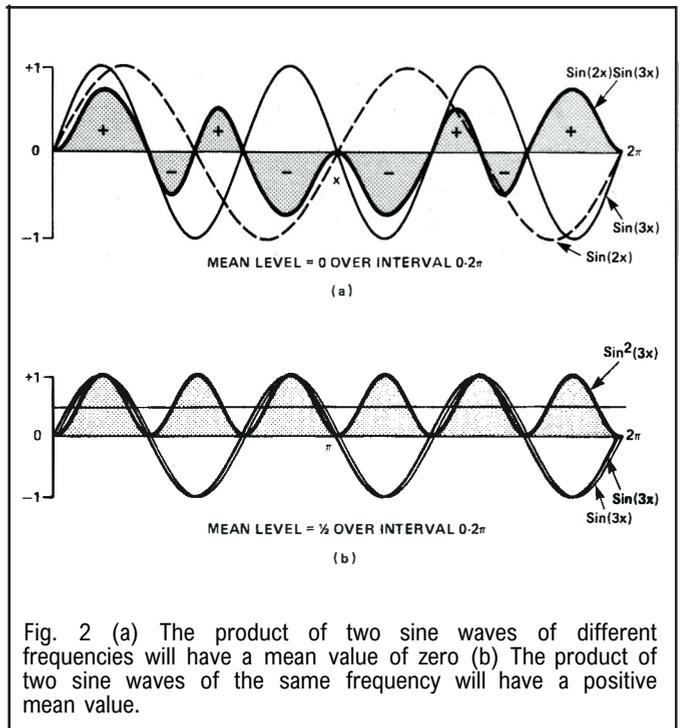


Fig. 2 (a) The product of two sine waves of different frequencies will have a mean value of zero (b) The product of two sine waves of the same frequency will have a positive mean value.

below the axis. Integrate and you get zero. How about  $\cos(9x)$  over the same interval (9 complete cycles)? Integrate, and that vanishes too.  $\sin(566,344,890x)$  over the same interval? You guessed it — integrate and it vanishes.

Now let's try something else. Take a sine wave, let's say  $\sin(2x)$ , and multiply it by another.  $\sin(3x)$ , for example. The result of this particular multiplication is shown in Fig. 2a. It's not certain from the drawing but it looks very much as if the two larger areas above the axis match the two larger areas below and similarly with the smaller areas. It looks as if this might disappear when integrated as well!

In fact, this is exactly what happens. It's beginning to seem as if just about any combination of sines and cosines will vanish over 0 to  $2\pi$ . The exception occurs when two sines or two cosines of the same frequency are multiplied together. Figure 2b illustrates this for  $\sin(3x) \times \sin(3x)$ . Since the resulting waveform is always positive, integrating will give a positive result.

This can all be summed up as follows:

$$\int_0^{2\pi} \sin(mx)dx = \int_0^{2\pi} \cos(nx)dx = 0 \quad (\text{for all } m, n)$$

$$\int_0^{2\pi} \sin(mx)\cos(nx)dx = 0 \quad (\text{for all } m, n)$$

$$\int_0^{2\pi} \sin(mx)\sin(nx)dx = \begin{cases} 0 & (\text{for } m \neq n) \\ \pi & (\text{for } m = n) \end{cases}$$

$$\int_0^{2\pi} \cos(mx)\cos(nx)dx = \begin{cases} 0 & (\text{for } m \neq n) \\ \pi & (\text{for } m = n) \end{cases}$$

where  $m, n$  are integers  $> 0$

The results are quite easy to prove. Integrating the product of two functions is a perfect pain but by making use of the identity  $\sin(mx)\cos(nx) = \frac{1}{2}(\sin(m+n)x + \sin(m-n)x)$  and similar identities for the product of two sines and of two cosines, the integrations can be performed without much difficulty.

The description 'orthogonal' (perpendicular) may seem an odd one to apply to sine waves. It arises from certain similarities between operations that can be performed on sines and operations that can be performed on vectors — in particular the scalar product of two vectors which vanishes when they are at right angles to each other.

The place where 'sine wave vectors' feel at home is called  $L_2$ . It's an abstract space with an infinite number of dimensions. It's one of a class of abstract spaces known as Hilbert spaces.

Imagine a set of axes, all at right angles to each other, each labelled  $\sin(x), \sin(2x), \sin(3x)$ , and so on. Now mark out on each axis the Fourier coefficient showing 'how much' of the sine wave of that particular frequency there is in the function of your choice. When you've finished marking out all the axes, you'll be able to place a point in the space which has just those co-ordinates (just like the  $x$  and  $y$  co-ordinates in the common or garden Cartesian system). So, each function with a Fourier expansion can be represented by a single point in  $L_2$ . Clever, eh? It's a fascinating place and we're taking holiday bookings now!

## Fishing For Sines

The orthogonality property is not just an incidental part of Fourier analysis, it's the key to the whole process. In this issue you'll find a circuit which will perform Fourier analysis by orthogonality. It's called a hi-fi power meter but don't be fooled by that!

The input side of the circuit is not needed for this argument. Take the components from the multiplier onwards (Fig. 3). At one input to the multiplier there is the waveform to be analysed. At the other input is a sine wave signal generator. If the signal generator is set to a frequency not present in the 'unknown' waveform, the average output from the integrator will be zero (for the same reason that the mean level of Fig. 2a is zero). If the sine wave exactly matches the frequency of one of the components of the unknown waveform, the output will have a DC component which will register on the meter (Fig. 4).

If you want to try this, start fishing with a low frequency sine wave. Increase the frequency of the bait until you see the meter move, showing that you've caught a sine. The meter will move quite violently, so use a cheap one and set it to centre scale. The movement of the meter will first occur when you are within a few Hz of the fundamental frequency. When you hit it exactly, the movement will stop. The meter reading will depend on the relative phase of the 'unknown' waveform and the bait.

Continue up the scale and you can determine the frequencies of other sine wave components. You know roughly where to look — they will be multiples of the

fundamental. With a square wave as the unknown, you won't find any even multiples. With other waveforms, other harmonics may be missing.

With some slight modifications to the integrator, and by displaying the output on a 'scope instead of a meter, you can determine the relative amounts of each harmonic. Setting the signal generator slightly off frequency will give 'beats' with an amplitude proportional to the 'amounts' of each component. If your signal generator has a sweep function and your scope an external trigger, you're in business with a complete spectrum analyser!

The sine wave and the 'unknown' should each have an amplitude of about 1V. To get satisfactory results on a sweep, the integrator will have to be replaced by a more suitable detector circuit. If you're not sure how to go about it, we hope to publish a complete spectrum analyser based on this principle sometime soon, so watch out for it!

## The Fourier Coefficients

Back to the maths again. What needs to be done now is to apply the same process mathematically as we've just done electronically. First of all, a reminder of the form of the Fourier series:

$$f(x) = a_0 + a_1\cos(x) + b_1\sin(x) + a_2\cos(2x) + b_2\sin(2x) + \dots$$

Now the bait. Suppose we want to know how much  $\cos(2x)$  there is in  $f(x)$  (in other words, we want to find the value of  $a_2$ ). Multiply the whole lot by  $\cos(2x)$  and integrate from 0 to  $2\pi$ :

$$\int_0^{2\pi} f(x)\cos(2x)dx = a_0 \int_0^{2\pi} \cos(2x)dx + a_1 \int_0^{2\pi} \cos(x)\cos(2x)dx + b_1 \int_0^{2\pi} \sin(x)\cos(2x)dx + a_2 \int_0^{2\pi} \cos(2x)\cos(2x)dx + b_2 \int_0^{2\pi} \sin(2x)\cos(2x)dx + \dots$$

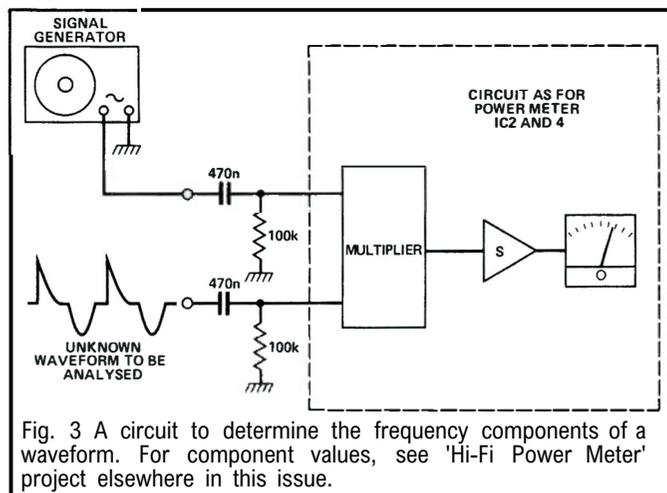


Fig. 3 A circuit to determine the frequency components of a waveform. For component values, see 'Hi-Fi Power Meter' project elsewhere in this issue.

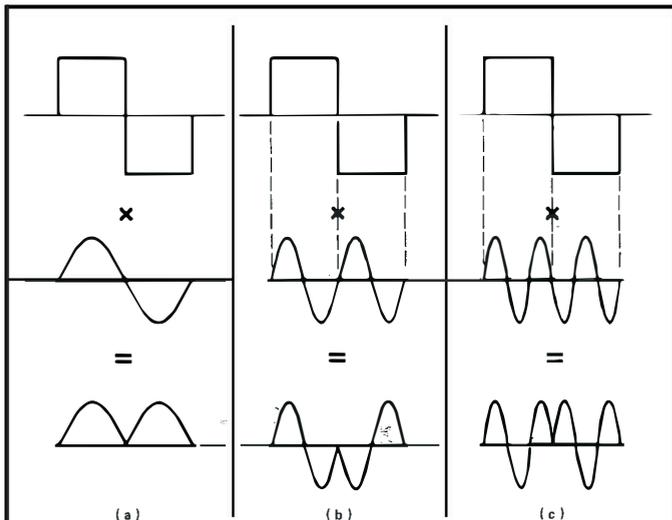
On the right hand side, every single term apart from the one involving  $\cos(2x)$  will disappear (check it out with the orthogonality integrals listed earlier). This is quite a relief as it means we don't have to do an infinite number of integrations! We are left with:

$$\int_0^{2\pi} f(x)\cos(2x)dx = a_2 \int_0^{2\pi} \cos(2x)\cos(2x)dx = a_2\pi$$

So the amount of  $\cos(2x)$  in  $f(x)$  is given by:

$$a_2 = \frac{1}{\pi} \int_0^{2\pi} f(x)\cos(2x)dx$$

If you think about the right hand side of this equation for a moment, it's doing exactly the same thing as the



**Fig. 4 Fishing for sines in a square wave. (a) Multiplying by the fundamental gives a positive 'output' on integration. (b) Multiplying by the second harmonic gives a wave with equal areas above and below the axis (there is no second harmonic present in a square wave). (c) Multiplying by the third harmonic gives a wave with more area above the axis than below — again, a positive output after integration.**

multiplying circuit. If there is no  $\cos(2x)$  in  $f(x)$ , then multiplying and integrating will give no 'output' and so the value of  $a_2$  will be zero. If there is some  $\cos(2x)$  present, the 'output' will be equal (in this case) to the value we will give to  $a_2$ .

The other coefficients are calculated in exactly the same way:

$$a_n = \frac{1}{\pi} \int_0^{2\pi} f(x) \cos(nx) dx \quad b_n = \frac{1}{\pi} \int_0^{2\pi} f(x) \sin(nx) dx$$

The only term not yet dealt with is  $a_0$ . To get this value, the Fourier series is integrated 'raw' — without multiplying it by anything — giving:

$$\int_0^{2\pi} f(x) dx = \int_0^{2\pi} a_0 dx$$

$$\text{so } a_0 = \frac{1}{2\pi} \int_0^{2\pi} f(x) dx$$

This month's article has been rather heavy on the maths side. (You noticed?) The most horrifying thing about maths is the thought that someone may put you on the spot and actually ask you to *do* some. It brings back all the examination nightmares: Question 19. Do the most horrible double integral you can think of over an arbitrary surface with knobby bits on, take away the number you first thought of and express the answer to 12 decimal places. Then keep doing it again 'till you get it right.

If you've forgotten most of the mathematical techniques for grinding out the 'right answers', don't worry. Next month there will be a practical example of how to 'do' a Fourier series. In the privacy of your own home you might find it easier than you think. Besides, if you get it wrong nobody will ever know!

For this month, if you have followed the ideas through, that's the main thing. If you have, we'd like to award you the ETI medal for dedication to your hobby above and beyond the call of duty. The only trouble is, the medal's in Hilbert space and we can't get it out!

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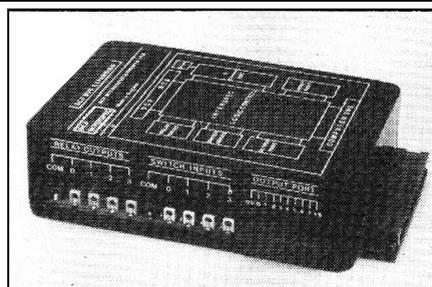
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The expansion bus provides all the data and address/control signals for the addition of further DCP modules or home-built devices. Connection is by multi-way PCB connector and all the information required

### INTERBEEB £49.95

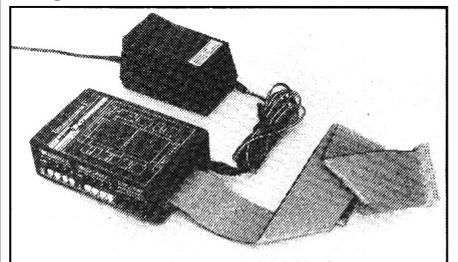
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- 8-bit output port
- four switch sensor inputs
- four relay-switched 12V 1A outputs
- eight channel multiplexed analogue to digital converter
- precision 2.5V reference
- external power supply
- 15-way expansion bus

All sections of the interface are memory mapped in the 1MHz expansion map for maximum ease of use and compatibility with existing peripherals.

The expansion bus provides all the data and address/control signals for the addition of further DCP modules or home-built devices. All the information required for using additional devices is included.





# RIAA EQUALISATION

Even with the advent of CD, analogue records are far from dead. Wilfred Harms explains how to design RIAA networks that will accurately replay your discs.

**R**IAA equalisation is an important feature of any amplifier designed to reproduce music from an analogue disc. Suitable circuit designs can be found in any number of published sources.

Unfortunately, the circuits contained in many handbooks, electronics journals and even inside some expensive pieces of audio equipment are often inaccurate. Incorrect designs are often repeated without question and the original requirements are simply forgotten.

This is a pity because it doesn't cost any more to use a resistor and capacitor of the correct value and the results are well worth the extra time and trouble. The purpose of this article is to show why RIAA equalisation is important and how to go about choosing the right filter components when designing disc equalisation networks.

## In The Groove

From the earliest days of electrical recording it has been standard practice to modulate record grooves using a constant-velocity recording characteristic and to replay the signal with a velocity-dependent pickup. The maximum velocity is set at a certain value and the amplitude of the signal voltage is varied with frequency so this maximum is always achieved.

The system is illustrated in Fig.1. The maximum velocity is represented by the greatest rate of change of signal voltage, the steepest part of the waveform slope. On a sine-wave this will always occur at the zero-crossing points.

On lower frequency signals, the maximum velocity will be less as the rising edge of the waveform is less steep. If, however, the amplitude of lower-frequency signals is increased, a point will be reached at which the rising edge is as steep as that of a higher frequency signal with lower amplitude. This is the principle on which constant velocity recording works, the maximum velocity remaining constant across the audio band while the amplitude varies according to the signal frequency.

The main drawback with this system is that bass frequencies require a very large amplitude. The result would be wide groove spacing and correspondingly little recording time on each disc. In addition, the comparatively small amplitude at high signal frequencies would yield a poor signal-to-noise ratio.

To overcome these problems, the basic constant velocity characteristic is modified to a constant-amplitude characteristic over certain parts of the frequency range by means of a corrective network.

In the early days this was done very much at the whim of individual record manufacturers and a number of different replay characteristics grew up side by side. In order to handle the different recording characteristics correctly amplifiers were fitted with a number of switch-

selectable equalisation networks. For example, the Leak Point One Plus valve preamplifier of the 1950s had no less than four disc replay settings.

The situation was eventually rationalised by agreement. British Standard 1928 (issued in 1955 and re-issued without changes in 1965) recommends a recording characteristic similar to that put forward by the Comité Consultatif International des Radiocommunications (CCIR) in Europe and the Recording Industries Association of America (RIAA). The latter term is the one most commonly used today.

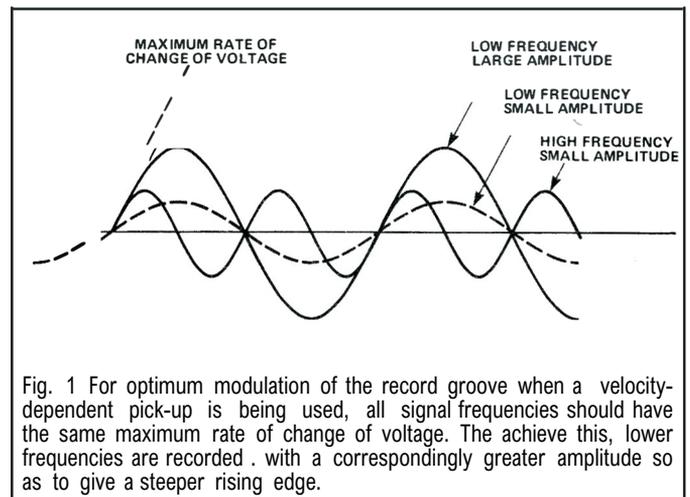


Fig. 1 For optimum modulation of the record groove when a velocity-dependent pick-up is being used, all signal frequencies should have the same maximum rate of change of voltage. To achieve this, lower frequencies are recorded with a correspondingly greater amplitude so as to give a steeper rising edge.

## Changing Shape

The RIAA characteristic modifies the basic constant-velocity characteristic to a constant amplitude characteristic at two points in the audio frequency band.

At very low frequencies the constant-velocity characteristic is retained so that the gain does not go on increasing right down to the lowest recorded frequencies. Using a constant-amplitude characteristic here would emphasise turntable rumble and vibration.

At bass frequencies the characteristic changes to constant-amplitude to limit groove pitch before switching back to a constant-velocity characteristic for the middle frequencies. At high frequencies the characteristic again becomes constant amplitude and remains so to the limits of the audio band.

These four distinct regions give the RIAA characteristic its familiar flat-steep-flat-steep shape. The shape is sometimes shown instead as a series of angular lines but these are merely asymptotes to the curves. Provided the recording and replay networks are as near identical as possible, the exact shape of the response does not make a lot of difference. It therefore makes sense to use a series of curves which can easily be

replicated to a high level of accuracy rather than an idealised, sharp-cornered response which could only be approximated with difficulty.

## Calculated Curves

The response shape is described in terms of three curves (flat becoming steep, steep becoming flat and flat becoming steep again) which 'turn over' at frequencies of 50.05Hz, 500.5Hz and 2.115kHz. The slope of the curves is that given by a first order (6dB/octave) filter network comprising one resistor and one capacitor.

The RIAA replay characteristic is the exact opposite of the recording characteristic and is shown in Fig. 2. The complete characteristic can, in theory, be reproduced using three capacitors and three resistors in series and parallel pairs, although this is not necessarily the best way of doing it as we shall see later.

The actual values of the resistors and capacitors used will vary according to the individual circuit configuration, but the CR time constant for each filter curve is determined solely by the turn-over frequency and is therefore fixed. For this reason, it is usual to define the three curves in terms of CR time constants.

The values required must, at the frequency concerned, give CR values which result in C and R having equal impedances. This can be determined from the formula:

$$CR = \frac{1}{2\pi f}$$

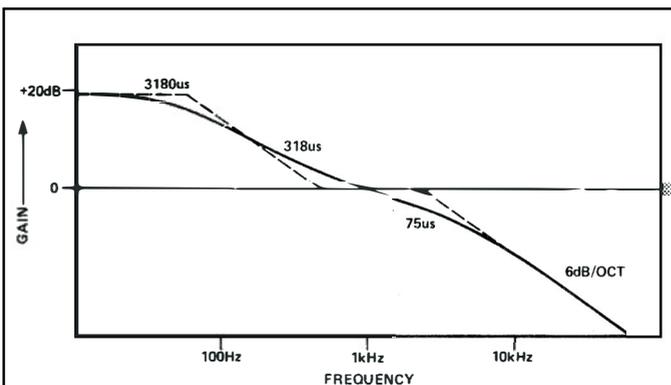


Fig. 2 The RIM replay characteristic.

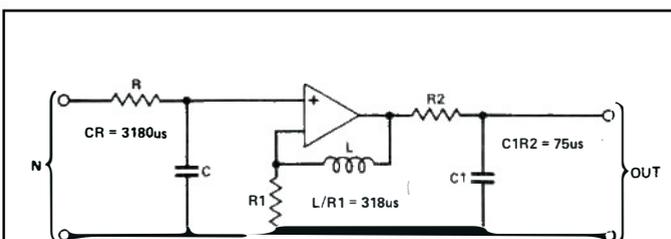


Fig. 3 A simple replay equalisation circuit using separate filter networks for each of the three time constants.

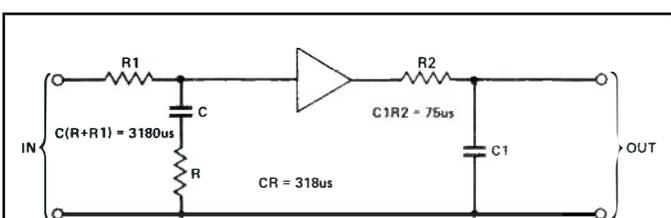


Fig. 4 A two-stage replay circuit in which one compound filter stage provides two of the time constants.

and for the RIAA characteristic gives time constants of 3180, 318 and 75 microseconds. These time constants are, incidentally, the period of one radian of one cycle at the frequency concerned.

Figure 3 shows a simple equalisation network which uses three separate stages to realise the RIAA characteristic. This will work but a much better approach is to merge two of the networks in the way shown in Fig.4.

In practice, all three stages are usually combined into a single network and some examples are shown in Fig.5. All of these circuits give similar results but in each case there will be a degree of interaction between the three time constants and this will affect all four circuit components.

The response curves for an RIAA network are defined in terms of a single reference frequency, 1kHz. Taking the circuit of Fig.4 as an example, the output level from the 318/3180μs section (the network comprising R, R1 and C) will be 11.17% of the input signal level. Similarly, the output from the 75μs section (the network comprising R2 and C1) will be 90.46% of the its input level.

Taking these two together, the final output level from the circuit at 1kHz will be (0.1117 x 0.9046 =) 0.10103 times the input level or 10.103%. Therefore the input or zero-frequency response for the network should be set at (1/0.10103 =) 9.898 times the reference response at 1kHz.

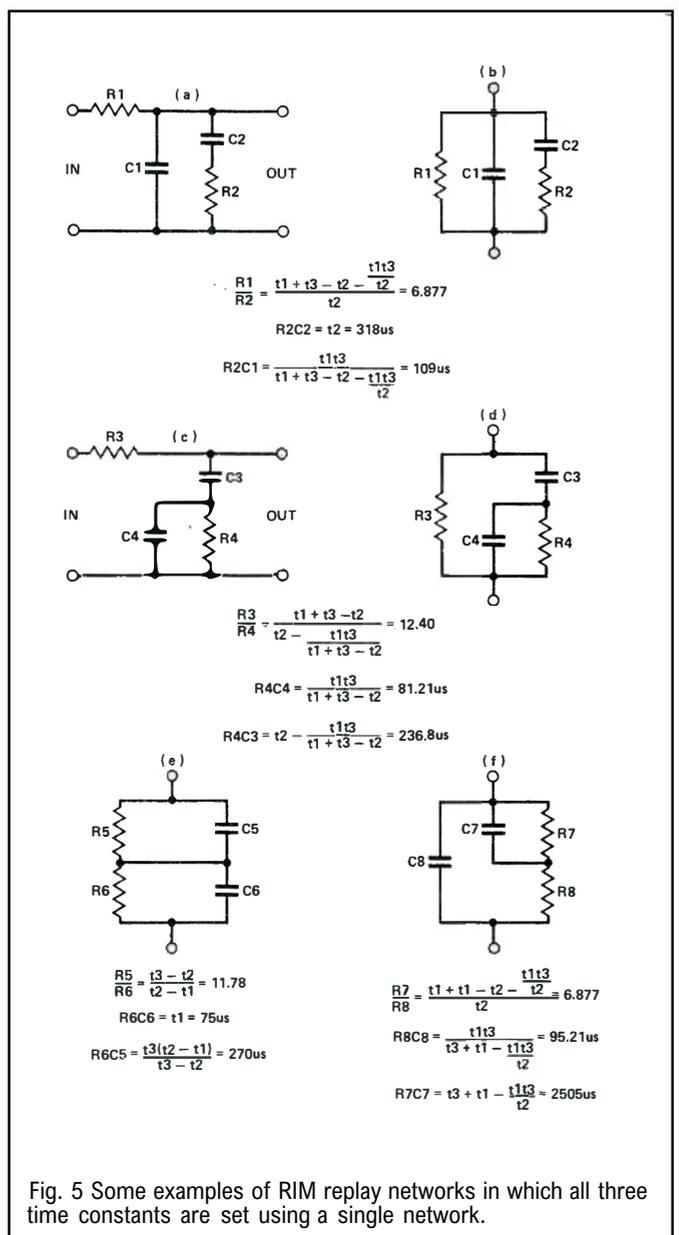


Fig. 5 Some examples of RIM replay networks in which all three time constants are set using a single network.

## Design Misconceptions

Figure 6a shows a type of network which is frequently used, and component values in similar proportions will be found in many RIAA circuits.

The zero-frequency impedance is 1M1 whilst the impedance at 1kHz is 122k which is too high. The result is a loss in response below 1kHz of up to 1dB.

Here  $R_5C_3 = 75\mu s$  and  $R_6C_4 = 3300\mu s$  which is acceptable. The error is in the false assumption that  $R_5C_4$  should equal  $318\mu s$ . A check with the basic formulae in Fig4(e) shows that  $R_6/R_5 = 11.78$ , and to meet this,  $R_6$  must be increased to 1M2 and  $C_4$  reduced to 2n7.

Readers may spot that this network appeared in ETI March 1986 in connection with the free PCB for use as a pre-amplifier with RIAA equalisation. The notation here agrees with the original diagram for recognition.

Figure 6b shows another commonly used RIAA network, and again it is possible to find component values in similar proportions in many other networks. As with the previous circuit, the impedance at 1kHz is high resulting in a loss in response at both lower and higher frequencies. Since  $R_5R_3 = 3300$ ,  $R_4C_3 = 330$  and  $R_4C_2 = 72.6$  what is wrong?

In this case everything because interaction affects all values. Fig4(d) requires that  $R_5C_3 = 2937\mu s$ ,  $R_6C_2 = 81.2\mu s$  and  $R_7/R_4 = 12.40$  and three components must be changed. If it is desirable to retain the 33k resistor, then suitable values for the others would be  $R_2 = 2.7k$ ,  $C_2 = 30n$  and  $C_3 = 91n$ .

Readers may recognise this network because it appeared in a clever valve pre-amplifier in ETI August 1986, and again the notation agrees with the original. A similar network for use with transistors by the same author appeared in ETI September 1986, and this can be modified in a similar fashion.

Out of interest, I have calculated the deviations from the RIAA standard found in the circuits of Figs. 6 and 7 and these are shown in Table 1.

The noticeable common error in faulty networks is that one of the two larger resistors is ten times the other, a circumstance which cannot arise if it is correctly designed.

The ratios of component values in Fig4 in terms of time constants ( $t_1 = 75\mu s$ ,  $t_2 = 318\mu s$ ,  $t_3 = 3180\mu s$ ) are those originally given by EMI Studios which have been checked and evaluated to facilitate their use. The theoretical differences appropriate to a feedback circuit are within the normal component tolerances (1% recommended) provided the 1kHz gain exceeds 65.

In conclusion, one must realise that the final design of any RIAA replay network depends upon the equalisation circuit as a whole and particularly upon the impedances associated with it. But perfection cannot be obtained without an understanding of the underlying principles.

	VLF	50kHz	150kHz	1kHz	10kHz	30kHz
Accurate RIAA replay response	19.91	16.95	10.27	0	-13.73	-23.12
Fig.6 response	19.20	16.07	9.37	0	-13.51	-22.89
deviation	0.71	0.68		0	0.22	0.23
Fig.7 response	19.00	15.62	8.70	0	-12.51	-21.84
deviation	0.91	1.33	1.57		1.22	1.28

Table 1

## Network Design

Designing a network of the type shown in Figs. 2 and 3 is quite straightforward but the single networks of Fig.4 require a different approach.

For those who want to go into the mathematics of it all, the figure for output level/input level of an RIAA network is given by

$$\frac{(1 + st_2)}{(1 + st_1)(1 + st_3)}$$

where  $t$  is the period of the CR time constant and  $s = j\omega$  ( $\omega$ , of course, is shorthand for  $2\pi f$ ). Taking the circuit of Fig.4a as an example, the output level/input level at a given frequency will be equal to

$$\frac{(1 + sR_2C_2)}{1 + s(R_1C_1 + R_2C_2 + R_1C_2 + s^2R_1R_2C_1C_2)}$$

The two expressions can be equated and the component ratios determined.

Thankfully, there is little need to go through all of this because a full set of data has been available for nearly thirty years. In *Wireless World* in 1957 W. H. Livvy of EMI Studios presented a set of formulae which allow the ratios between resistor and capacitor values to be determined accurately for different time constants. Two of the networks, he suggested, were suitable for passive de-emphasis but all could be used in feedback circuits because the overall impedance/frequency variations were in accordance with the RIAA requirements.

The data is presented in an even simpler and more readily-useable form in a technical paper written by Peter Baxandall. Entitled 'Pick-Up Equalisation' it appears in the *Radio, TV and Audio Technical Reference Book* edited by S. W. Amos (Newnes-Butterworth, 1977). Baxandall uses formulae for the component ratios based on the original 1957 data and describes the operation and use of several types of network. The article is just five pages long yet it covers not only the networks but also such questions as where the equalisation should be placed, the problem of inverted feedback, aspects of pick-up response correction and sensitivity and the minimum levels of gain in feedback circuits.

## Network Accuracy

If the accuracy of an RIAA network is to be assessed against the published standard it is helpful to be able to calculate the response figures in decibels. The formula for any frequency,  $f$ , is

$$10_{\log} \frac{441.18 (r^2 + 0.2505)}{(100r^2 + 0.2502)(r^2 + 4.503)} \text{ dB}$$

where  $r = f/1000$ . If it is desired to check the characteristic of one network against another, the impedance must first be determined at any frequency and compared with the impedance at 1kHz to give

$$20_{\log} \frac{Z}{Z_{1k0}}$$

Unfortunately, the calculations are far from easy!

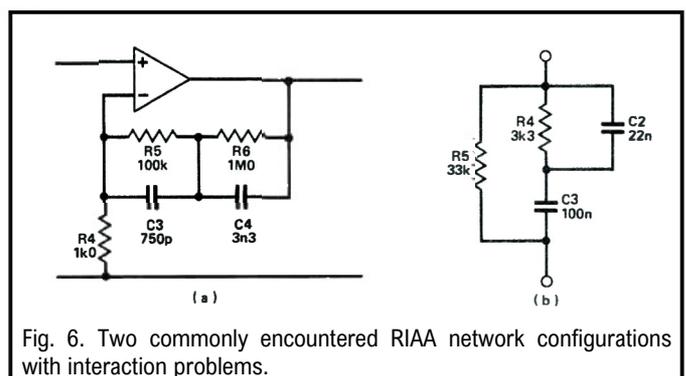


Fig. 6. Two commonly encountered RIAA network configurations with interaction problems.

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**MK12 IR Receiver (incl. transformer) £14.85**  
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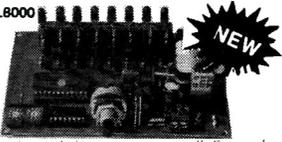
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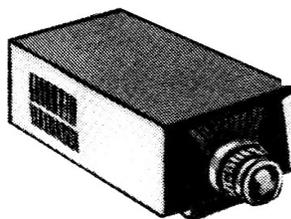
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# FLAT ALARM

No, not a warning for punctures. Barry Thurlow's device is a full specification, but compact and cheap security system for a flat or small house.

**M**ost burglar alarms on the market are aimed at the industrial market, a fact that is amply reflected in their price. Many commercial alarms also suffer from the problem that they are difficult to set. The user either has to wait for a fixed time to be sure the alarm is set or he is given no indication at all that the device has been successfully 'armed'.

This design attempts to solve this problem at a low cost and provides an alarm bell with all the required features. The prototype has been in use for over a year and has proved both effective and reliable for all this time.

## Features

The features offered are summarised as follows:

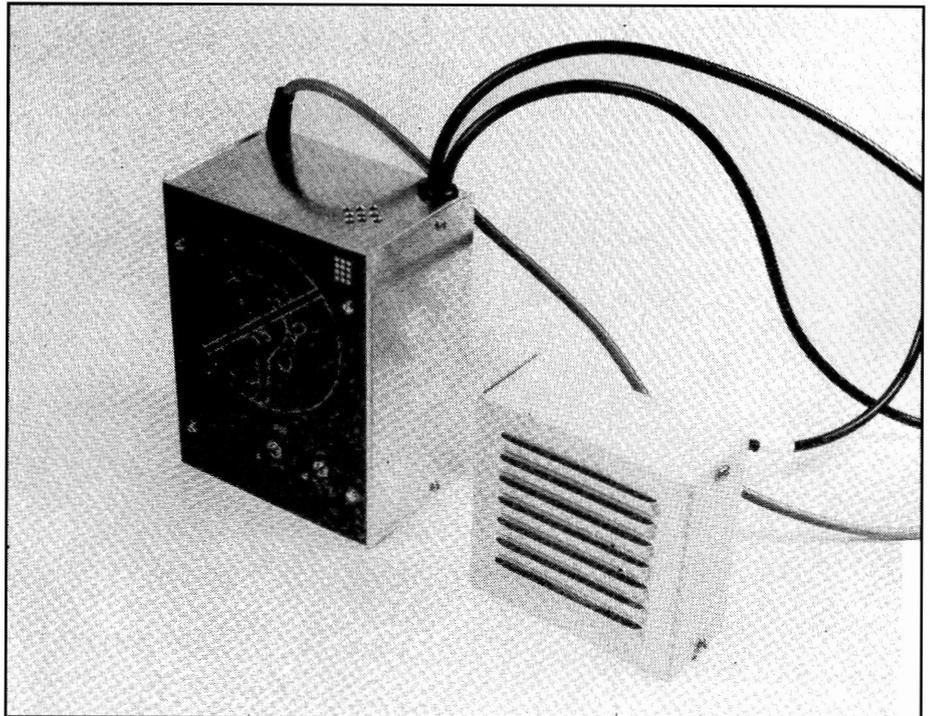
- LED flash to indicate operation of the timing circuit.
  - Audible signals for setting.
- The warning buzzer sounds when the door is opened to leave the premises and stops immediately the circuit is completed.
- 42 second entry delay giving time to reset the system.
  - Siren cancelled after 24 mins.
  - Battery backup to prevent disabling by cutting mains.
  - Facilities to include both

normally open and normally closed type detectors.

The Flat Alarm uses two detector circuits: one of normally closed contacts in series and (optionally) one of normally open contacts in parallel. Either breaking the normally closed circuit or closing the normally open one will activate the alarm.

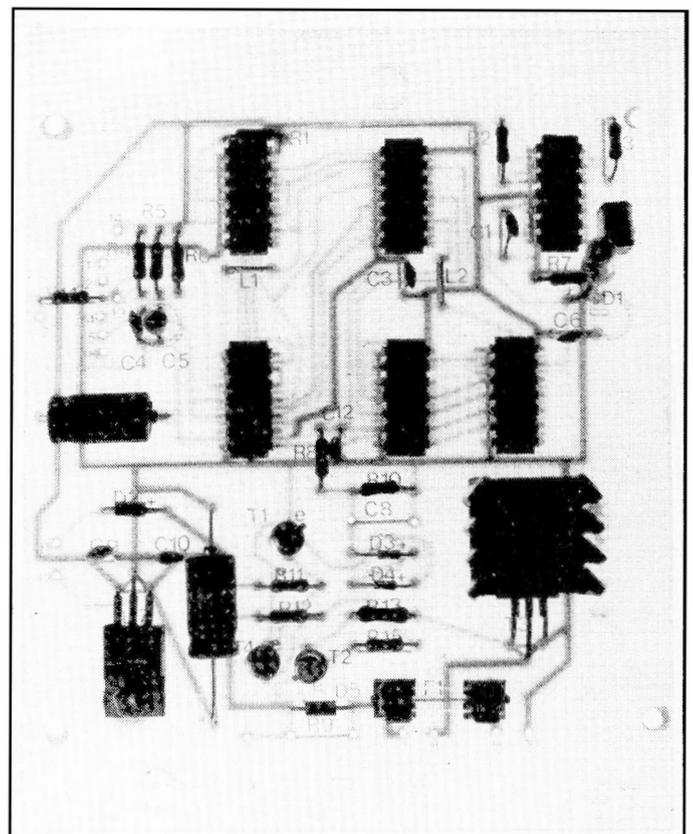
The detector switches can be any number of a variety of different types. Everything from simple sprung door switches to floor pressure mats and window foil strips are easily available and can be connected to the system.

The switches designed for a car courtesy light, operated by the door can provide a useful and cheap source for both door and window detectors.



Above: the complete Flat Alarm with the 12V siren.

Right: the Flat Alarm PCB ready for wiring up in the case.



# PROJECT

All wiring to the detector switches can be simple 'bell' cable and should be kept concealed as it runs around doors and windows to discourage tampering. In case a particularly ingenious intruder cuts the mains supply before attempting access, the Flat Alarm has a backup battery power supply.

Unlike most alarm systems the Flat Alarm uses no arming switch requiring a mad dash for the front door after it is closed. Instead this system has a simple on/off switch. In the on position ('armed') the detector switch on the front door acts as the alarm set.

Once the door has been opened and then closed (as you

leave) the alarm is armed. An internal buzzer indicates that the alarm is set while the door is open. Any further break in the circuit will trigger the siren (after a 42 second pause for resetting the system for when the 'break-in' is actually you returning).

The siren is also turned off 24 minutes after starting for the sake

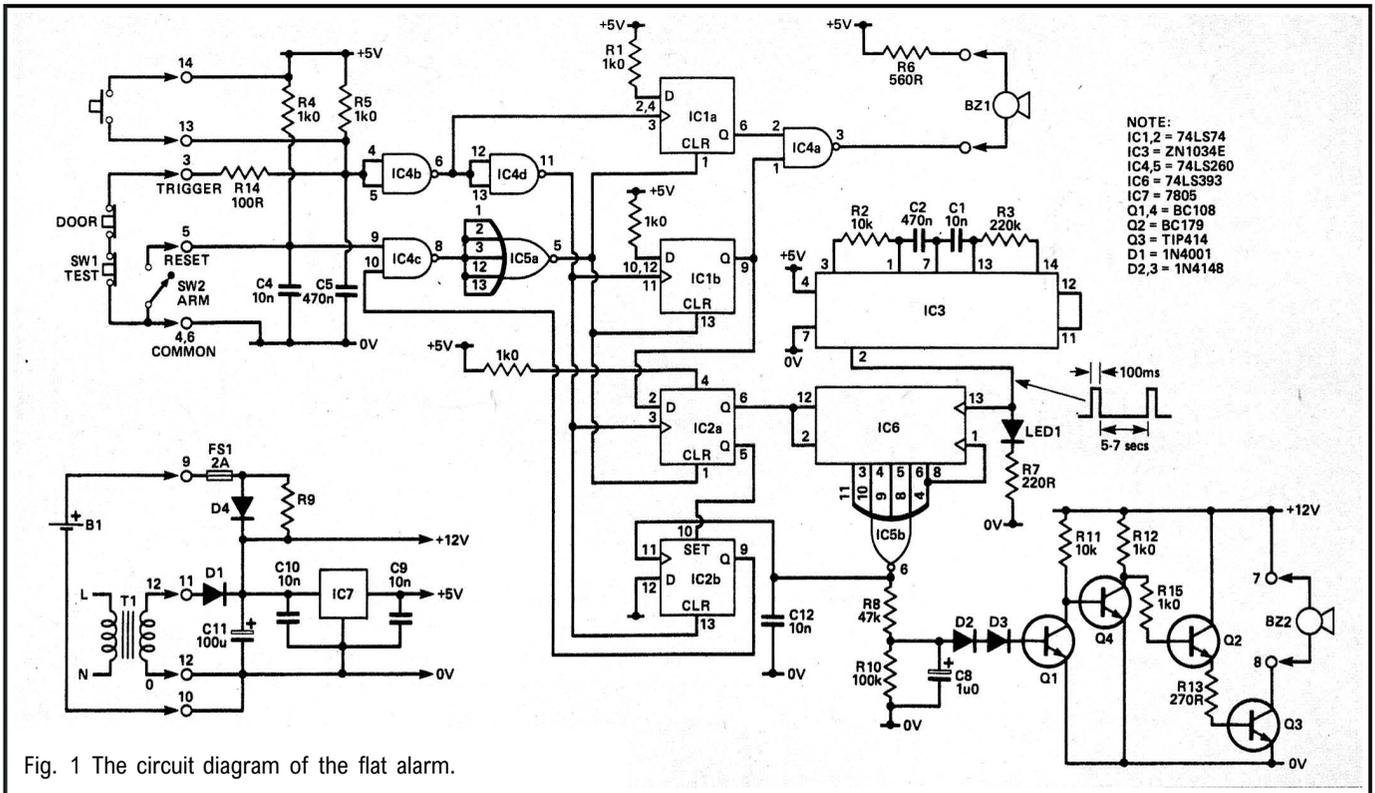


Fig. 1 The circuit diagram of the flat alarm.

## HOW IT WORKS

The circuit is shown in Fig. 1 and may be considered in a number of blocks.

The transformer, T1, D1 and C11 form a simple unregulated 15V supply. This supply is regulated by IC7 to supply 5V to the logic. D4 allows current to be supplied from the battery to power the siren and, if the mains is off, IC7 as well. R9 provides the charging current for the battery while the mains supply is on.

C4 and C5 are for noise suppression on the trigger inputs.

Three flip-flops IC1a, IC1b and IC2a form an escapement trigger mechanism. When the detector (assumed to be a normally closed switch, across terminals 3 and 4 of the PCB) is opened (the owner opening the door to leave) a rising edge is presented on pin 11 of IC1b. This clocks a high to the output pin 9 which passes through the NAND gate (IC4a) to sound the warning buzzer, BZ1.

The rising edge on IC2a pin 3 only serves to keep IC2a in the same state since the level on its input (pin 2) at the clock time was a low.

When the detector is closed (the owner leaving) a rising edge is presented on IC1a pin 3. This clocks the high on its input to the inverted output (pin 6) as a low. This sets the output of the NAND gate to high, silencing the buzzer.

If the detector is open again (the owner returning or a burglar entering) a rising edge on pin 3 (IC2a) clocks the signal at its input (now high) to the outputs. The resultant low on IC2a pin 6 enables the counter, IC6. IC6 provides the counting for the entry delay and the auto shut off after 24 minutes.

The basic timing for the alarm comes from IC3. This is a free running R-C oscillator and 12 stage counter configured to provide a stream of pulses approximately 100ms in width at a rate of about one every six seconds.

The correctness of the timing pulses may be checked by viewing LED1 which pulses on in time.

The six second pulses are counted by an eight stage counter, IC6. The outputs of IC6 are decoded by the NOR gate IC5. Outputs A,B,C from the counter are not connected to the NOR gate and so the first seven pulses counted have no effect on the output. These seven pulses, amounting to some 42 seconds, constitute the entry delay.

If the reset switch is pressed within this time delay no further action will take place. Outputs D,E,F,G,H of the counter

are decoded by the NOR gate so that any count between 8 and 255 will produce an output. This is the time for which the siren will sound.

After 255 counts (around 24 minutes) the output pin 6 of the NOR gate will become high. This silences the siren and clocks the flip-flop IC2b producing a reset signal on IC2b pin 9. This sets the circuit back to its initial condition.

The signal from IC5 pin 6 is amplified by the transistor circuit comprising Q1 to Q4 to provide about 500mA for the siren. To activate the siren the voltage IC5 pin 6 is taken low. Diodes D3 and D4 provide an offset to allow for the offset of the logic low signal from the gate Q1 will be switched off and current will now flow through R11 into the base of Q4 about 1mA is provided which keeps Q4 saturated whilst drawing about 10mA through R12 and 10mA from the base of Q2 via R15. The base current in Q2 keeps it saturated whilst providing a base current for Q3 of 40mA. The switching gain of Q3 is greater than 20, and so it will be held in saturation for a siren current of 500mA.

C8 is provided to start up the siren slowly and should be omitted if a bell is used instead of the recommended siren.

# PROJECT

of the neighbours and in accordance with the recommendations of the noise abatement society. If the recommended electronic siren is used this feature will be much appreciated!

## Construction

All the ICs and discrete components are mounted on the PCB. The warning buzzer, transformer and battery are mounted in the case with flying leads to the PCB. Connection to the detector circuits, siren and reset switch is also by flying lead although the constructor may wish to fit a terminal block to make connection more convenient.

Connections to the PCB are as follows:

- 1 warning buzzer negative.
- 2 warning buzzer positive.
- 3/4 detector circuit for normally closed type detectors.
- 7 siren positive.
- 8 siren negative.
- 9 battery positive.
- 10 battery negative.
- 11/12 transformer secondary.
- 13/14 detector circuit for normally open detectors.

The PCB is designed to be mounted on pillars facing the front panel of the case. In this position the LED can be made to show through the front panel by

extending its leads. To mark the case for drilling place the blank PCB on the front of the case with the component side facing upward. Use a pin to mark

## PARTS LIST

<b>RESISTORS (all 1/4W, 5% unless specified)</b>		IC6	74LS393
R1,4,5,12,15	1k0	IC7	7805
R2,11	10k	Q1,4	BC108
R3	220k	Q2	BC179 or BC478
R6	560R	Q3	TIP41A
R7	220R	LED1	Red 0.2in LED
R8	47k	D1,4	1N4001
R9	100R 1W	D2,3	1N4148
R10	100k	<b>MISCELLANEOUS</b>	
R13	280R 1/2W	B1	12V 1.2amp-hour lead-acid battery
R14	100R	BZ1	High power piezo buzzer
<b>CAPACITORS</b>		BZ2	12V siren
C1,3,4,6,9,10,12	10n	FS1	2A fuse and PCB-mount holder
C2	470n	SW1	SPST push to break switch
C5	4u7 16V tantalum	SW2	SPST switch
C7,11	100u 25V axial electrolytic	T1	12V mains transformer
C8	1u0 25V axial electrolytic	<b>PCB: NO and NC detectors; connecting wire; 10-way terminal block; TO66 heat-sink; case; 20mm PCB standoffs; nuts, bolts and washers.</b>	
<b>SEMICONDUCTORS</b>			
IC1,2	74LS74		
IC3	ZN1034		
IC4	74LS132		
IC5	74LS260		

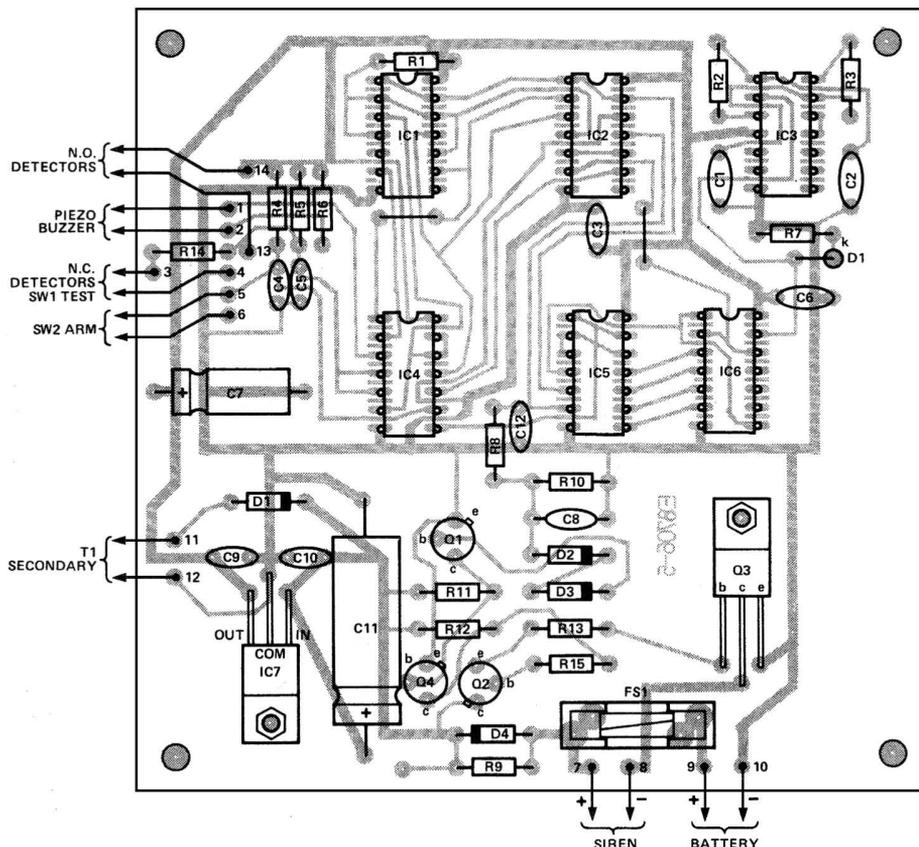


Fig. 2 The component overlay of the flat alarm.

through the four corner holes and through the two holes for LED1. Drill the corner holes with a 3mm drill centering the drill on the pin marks. Drill the hole for the LED using a 5.5mm drill. Centre the drill halfway between the two pin marks for LED1. When fitting the LED in, place an 18mm long sleeve over each of its leads to obtain the correct height. The PCB is mounted 22mm from the panel by the use of 20mm stand-offs and locking washers.

## Installation

The burglar alarm may be used with a combination of normally open contact detectors and normally closed contact detectors by connection to the appropriate pin pairs on the PCB. If no normally closed contact detectors are fitted, pins 4 and 3 should be joined together with a wire. If only normally closed type detectors are used, pins 13 and 14 are left unconnected.

It is often a requirement to wire alarm detectors in zones. For example, if the lower doors and windows of a house are to be alarmed but the upstairs windows are to be left open, provision must be made to bypass the sensors in groups. For normally closed contact detectors, the detectors are wired in series and the bypass switch must be in parallel with the group. For normally open contact detectors, the detectors are wired in parallel and the bypass switch is placed in series with the group (see Fig. 3).

Note that no reverse voltage protection is provided for the siren output on the PCB. If you use an inductive sounder (such as a bell) it is advisable to fit a protection diode across the PCB terminals 7 and 8, with the anode connected to terminal 7.

## Testing

First double check that all the components are correctly mounted. Check particularly for the polarity of the diodes and capacitors and for the orientation of the ICs. When this is done connect the transformer and power up the circuit.

Using a meter check the voltage on the power pins of the ICs. Pin 14 of IC1, IC2, IC4, IC5, IC6 and pin 4 of IC3 should be at +5V. Switch off and connect the battery taking care to get the polarity correct.

Connect the siren, warning buzzer, reset switch, and a sample detector. Use a normally closed type. Reset the circuit by

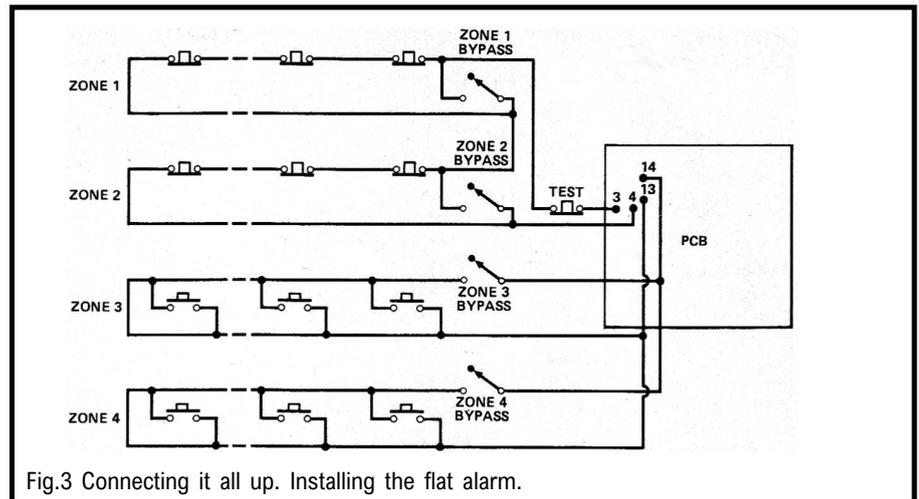


Fig.3 Connecting it all up. Installing the flat alarm.

closing the reset switch. Open the reset switch with the detector contacts closed. Check that the LED is pulsed about once every six seconds. Open the detector contacts and the warning buzzer should sound. Close the detector contacts. The warning buzzer should be silenced.

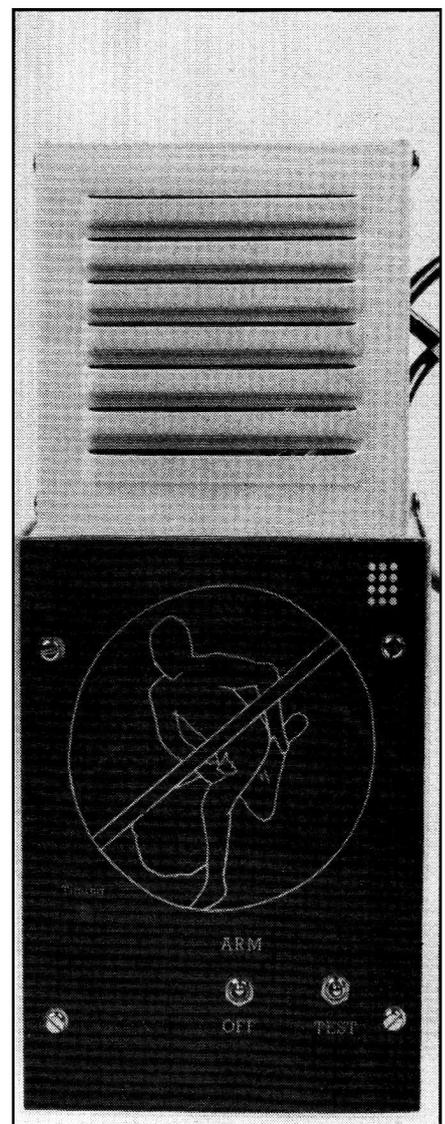
Wait 60 seconds to be sure that the alarm is armed and that the trigger has not been incorrectly activated. Nothing should happen. Open the detector contacts again and wait. After about 42 seconds the siren should go off.

If using the recommended siren this will be extremely loud so for testing it is advised that a pillow be placed over the siren to avoid ear damage!

After a further 24 minutes or so the siren should be silenced. If the detector is now closed and opened the warning buzzer will sound. This would indicate to the returning owner that the alarm has sounded and timed out while he was away. However this might only indicate that a window had been blowing in the wind and causing false alarms.

If the timings are not right check the components around IC3 for their correct values and positions.

If the siren does not sound or is weak although the warning buzzer worked as expected you may have a flat battery and this and the charging circuitry should be checked.



## BUYLINES

The high power piezo buzzer is available from Maplin (number FK84F) as are the lead-acid battery (number YJ69A) and the siren (number XG14Q). The siren is supplied in its own waterproof case.

The box for the main PCB is not critical and can be any suitable case which is able to contain the PCB, battery and test and reset switches and can be

hidden discretely near the door.

The PCB and the front panel label shown on the prototype are available from the author for £9.95 and £4.45 respectively, plus 50p post and packing. Orders should be sent to B.J. Thurlow, 3 Broadway House, Bromley Road, Downham, BR1 4PA.



Project	Month	Year	Page	Project	Month	Year	Page
Ignition timing light	Sep	1974	18	Drum synthesiser (Cymbal Synth) errata	Jun	1986	55
LED tachometer	Jan	1981	49	Drum synthesiser, ETI Staccato	Jun	1980	84
Light activated tachometer	Feb	1979	50	Drum synthesiser, ETI Staccato errata	Aug	1980	13
Light wand	Mar	1982	73	Drum synthesiser, midi	May	1984	62
Meter beater	Feb	1975	28	Drum synthesiser, midi errata	Aug	1984	66
Over speed alarm	Sep	1979	79	Drum synthesiser, mini	Nov	1983	36
Parking meter timer	Jan	1982	29	Drum synthesiser, mini errata	Apr	1984	62
Patch detector (Short Circuit)	Jan	1977	33	Ezeko spring-line reverbation unit	Oct	1984	18
Revealer - body filler detector	Aug	1973	58	Electronic bongos (Short Circuit)	Aug	1977	24
Rev monitor/counter	Dec	1977	37	Flanger / chorus unit	Jan	1984	33
Screen heater controller	Sep	1979	89	Flanger, The Better	Jan	1987	47
Smart battery charger	Jul	1981	85	Flanger, The Better errata	Mar	1987	63
Tacho / dwell, combined	Jan	1987	62	Fuzz box (Short Circuit)	Apr	1977	48
Tachometer	Jul	1977	32	Fuzz / sustain box	Oct	1980	53
Tachometer errata	Sep	1977	8	Fuzz / sustain box errata	Sep	1982	57
Tachometer, digital	Jan	1979	23	Guitar attack delay unit	Jun	1973	30
Tachometer, light activated	Feb	1979	50	Guitar effects unit	Apr	1979	97
Tacho timing light	Dec	1974	18	Guitar effects unit errata	Jun	1979	9
Trafficator flasher	May	1975	46	Guitar note expander	Apr	1981	95
Turn indicator canceller	Apr	1973	70	Guitar tuner	Jan	1982	41
Warning indicator monitoring System	Sep	1979	23	Guitar tuner errata	Mar	1982	9
Wiper delay, automatic	Jan	1986	50	Guitar tuner errata	May	1982	11
<b>MUSIC AND EFFECTS</b>				Gunshot sound effect	May	1982	89
				Hand-clap synthesiser	Aug	1981	68
				Metronome, accentuated	Feb	1978	17
				Metronome, accentuated beat	Jun	1979	21
				Metronome and beat counter (ETI Rhythm ROM)	Nov	1985	33
				Metronome and beat counter errata	Jun	1986	55
				Metronome, audio visual	Nov	1972	47
				Metronome (Free PCB project)	Nov	1980	56
				Metronome (Short Circuit)	May	1977	39
				Midi drum synth	May	1984	62
				Errata	Aug	1984	66
				MIDI-to-CV converter	Jun	1986	29
				Mini drum synthesiser	Nov	1983	36
				Mini drum synthesiser errata	Apr	1984	62
				Mini Synth (complex sound generator)	Oct	1978	17
				Multi-option siren	Jan	1981	22
				Musical box	Apr	1981	50
				Music box, MPU (ETI Twonky)	Feb	1979	79
				Music board for the ZX81 part 1	Apr	1983	16
				Music board for the ZX81 part 2	May	1983	54
				Music board for the ZX81 errata	Jun	1983	15
				Music processor	Nov	1981	38
				Music processor errata	May	1982	11
				New sound for your guitar	Jun	1973	30
				Noise gate	Jul	1985	38
				Noise generator	Dec	1979	67
				Noise gate with compressor and DI box	Dec	1985	46
				Organ, ETI Victory part 1	Feb	1983	19
				Organ, ETI Victory part 2	Mar	1983	36
				Organ, ETI Victory part 3	Apr	1983	56
				Organ, ETI Victory part 4	May	1983	67
				Organ, touch	Dec	1976	41
				Phaser	Dec	1976	29
				Phaser, CCD	May	1978	57
				Phaser / explosion sound effect	May	1982	63
				Phase / Waa unit	Jun	1981	24
				Playmate guitar effects amplifier part 1	Aug	1982	28
				Playmate guitar effects amplifier part 2	Sep	1982	16
				Polyphonic keyboard controller	Jul	1979	36
				Reverberation unit, solid state	Apr	1982	101
				Reverberation unit, spring line	Dec	1974	46
				Reverberation unit, spring line	Oct	1984	18
				Rhythm Chip, the (ETI Rhythm ROM)	Nov	1985	33
				Rhythm Chip, the (ETI Rhythm ROM) errata	Jun	1986	55
				Sequencer for Spectrum (ETI Spec Drum)	Dec	1985	41
				Simple echo unit (ETI Ezeko)	Oct	1985	18
				Sonneti combo amplifier	Mar	1985	22
				Sonneti combo amplifier errata	Jul	1985	27
				Sonneti CCD delay line effects board	Apr	1985	57
				Sorcerer string synthesiser part 1	Aug	1985	36
				Sorcerer string synthesiser part 2	Sep	1985	48
				Sorcerer string synthesiser part 3	Oct	1985	32
				Sound bender (ring modulator)	Oct	1981	88
				Sound effects 1: bomb drop	Apr	1982	50
				Sound effects 2: steam train and whistle	Apr	1982	118
1024-note composer (synthesiser sequencer)	May	1981	36				
Accentuated metronome	Feb	1978	17				
Accentuated beat metronome	June	1979	21				
Activator (aural exciter)	Jan	1986	30				
Activator errata	Jul	1986	56				
Audio phaser	Dec	1976	29				
Audio visual metronome	Nov	1972	47				
Auto chord rhythm generator part 1	Nov	1978	56				
Auto chord rhythm generator part 2	Dec	1978	80				
Better Flanger, the	Jan	1987	47				
Better Flanger errata	Mar	1987	63				
Black hole chorales	May	1980	90				
Black hole chorales errata	Sep	1980	11				
Bomb drop sound effect	Apr	1982	50				
Bongo box	Dec	1986	43				
Bongos, electronic	Aug	1977	24				
CCD delay line effects board, ETI Sonneti	Apr	1985	57				
CCD phaser	May	1978	57				
CCD phaser errata	Jul	1978	7				
Chorus / flanger	Jan	1984	33				
Chorus unit	Nov	1985	48				
Chorus unit errata	Jun	1986	55				
Chorus unit (ETI Black Hole)	May	1980	92				
Chorus unit (ETI Black Hole) errata	Sep	1980	11				
Combo amplifier, ETI Sonneti	Mar	1985	22				
Combo amplifier errata	Jul	1985	27				
Complex sound generator (Mini Synth)	Oct	1978	17				
Compression gate, direct inject	Dec	1985	46				
CV adaptor for MIDI controllers	Jun	1986	29				
Cymbal synth	Nov	1985	58				
Cymbal synth errata	Jun	1986	55				
Delay line, CCD	Apr	1985	57				
Delay line, digital part 1	Dec	1984	16				
Delay line, digital part 2	Jan	1985	62				
Delay line, digital part 3	Feb	1985	24				
Delay line, digital errata	Aug	1985	62				
Digital sound sampler part 1	Nov	1985	63				
Digital sound sampler part 2	Jan	1986	47				
Digital sound sampler part 3	Feb	1986	42				
Digital sound sampler part 4	Mar	1986	44				
Digital sound sampler part 5	Jun	1986	48				
Digital sound sampler part 6	Jul	1986	44				
Digital VCO	Mar	1985	16				
Digital VCO errata	Jul	1985	27				
Direct inject compression gate	Dec	1985	46				
Direct injection box	Sep	1985	43				
Drum machine	Apr	1981	75				
Drum sequencer for the Spectrum	Dec	1985	41				
Drum synthesiser for the Commodore 64 (Bongo Box)	Dec	1986	43				
Drum synthesiser (Cymbal Synth)	Nov	1985	58				

Project	Month	Year	Page	Project	Month	Year	Page		
Sound effects 3: phaser/explosion	May	1982	63	<b>PHOTOGRAPHIC</b>					
Sound effects 4: gunshot	May	1982	89						
Sound sampler, digital part 1	Nov	1985	63						
Sound sampler, digital part 2	Jan	1986	47		Automatic contrast meter	Apr	1982	39	
Sound sampler, digital part 3	Feb	1986	42		Automatic contrast meter errata	Jul	1982	35	
Sound sampler, digital part 4	Mar	1986	44		Electronic flash trigger	Jun	1975	42	
Sound sampler, digital part 5	Jun	1986	48		Enlarger exposure meter	Nov	1985	54	
Sound sampler, digital part 6	Jul	1986	44		Enlarger timer	Oct	1981	78	
Spec Drum sequencer	Dec	1985	41		Exposure meter	Feb	1976	46	
Steam train and whistle sound effect	Apr	1982	118		Flash sequencer	Aug	1981	57	
String Thing (Transcendent DPX) part 1	Aug	1979	18		Flash sequencer	Jul	1983	63	
String Thing (Transcendent DPX) part 2	Sep	1979	62		Flash sequencer errata	Aug	1983	70	
String Thing (Transcendent DPX) part 3	Oct	1979	35		Flash trigger	Dec	1979	97	
String Thing (Transcendent DPX) part 4	Nov	1979	64		Flash trigger	Oct	1980	30	
Sustain fuzz box	Oct	1980	53		Flash trigger	Jul	1983	70	
Sustain fuzz box errata	Sep	1982	57		Photographic process timer	Aug	1972	38	
Synthesiser, ETI 3600 part 1	May	1975	42		Photo process controller	Feb	1987	41	
Synthesiser, ETI 3600 part 2	Jun	1975	32		Photo timer	Sep	1975	11	
Synthesiser, ETI 3600 part 3	Jul	1975	54		Printimer - 1½ - 3 minute timer	Nov	1974	44	
Synthesiser, ETI 3600 part 4	Oct	1975	41		Printimer - 1½ - 3 minute timer errata	Dec	1974	71	
Synthesiser, ETI 3600 errata	Jan	1976	84		Process timer	Jan	1980	71	
Synthesiser, ETI 4600 part 1	Jan	1974	20		Shutter timer	Feb	1978	57	
Synthesiser, ETI 4600 part 2	Feb	1974	24		Slave flash	May	1972	48	
Synthesiser, ETI 4600 part 3	Mar	1974	40		Sound / light flash trigger	Aug	1976	46	
Synthesiser, ETI 4600 part 4	Apr	1974	44		Sound operated flash	May	1972	44	
Synthesiser, ETI 4600 part 5	May	1974	54		<b>RADIO</b>				
Synthesiser, ETI 4600 part 6	Jun	1974	24						
Synthesiser, ETI 4600 part 7	Jul	1974	52			80 metre direct conversion receiver part 1	May	1986	40
Synthesiser, ETI 4600 part 8	Aug	1974	58			80 metre direct conversion receiver part 2	Jun	1986	44
Synthesiser, ETI 4600 part 9	Sep	1974	48			Aerial matcher for SW receivers	Apr	1974	31
Synthesiser, hand clap	Aug	1981	68			Antenna controller	Jun	1981	78
Synthesiser, polyphonic part 1	Dec	1980	87			Air band converter	Dec	1979	76
Synthesiser, polyphonic part 2	Jan	1981	77			AM/FM radio	Nov	1984	21
Synthesiser, polyphonic part 3	Feb	1981	32			Errata	Jul	1985	27
Synthesiser, polyphonic part 4	Mar	1981	27			Chipmunk FM / AM radio	Jun	1978	79
Synthesiser, Project 80 - Dual VCA	Aug	1980	78			Chipmunk FM / AM radio errata	Jul	1978	7
Synthesiser, Project 80 - monitor amplifier	Oct	1980	79	Crystal calibrator		Mar	1981	39	
Synthesiser, Project 80 - noise generator	Apr	1981	59	Digital radio dial		Jan	1979	49	
Synthesiser, Project 80 - PSU, VCO and VCLFO	Feb	1980	62	FM stereo tuner part 1		Feb	1987	46	
Errata	Mar	1980	15	FM stereo tuner part 2		Mar	1987	34	
Synthesiser, Project 80 - VC envelope shaper	Jul	1980	88	Headphone radio, AM		Aug	1976	34	
Synthesiser, Project 80 - VC envelope shaper	Sep	1980	93	Low distortion stereo decoder		Feb	1987	46	
Synthesiser, Project 80 - VCF	May	1980	20	Marker generator		May	1976	25	
Synthesiser, Project 80 - VCM	Mar	1980	87	One-chip radio		Jan	1973	16	
Synthesiser, Project 80 - VC state variable filter	Jul	1980	84	RF attenuator		Sep	1976	62	
Synthesiser sequencer	May	1981	36	RF power meter		Oct	1978	30	
Synthesiser, string (ETI Sorcerer) part 1	Aug	1985	36	Speech compressor		Oct	1979	47	
Synthesiser, string (ETI Sorcerer) part 2	Sep	1985	48	Star Trek radio		May	1978	62	
Synthesiser, string (ETI Sorcerer) part 3	Oct	1985	32	Tic-Tac radio		Nov	1975	35	
Synthesiser, Transcendent 2000 part 1	Jul	1978	38	Two metre power amplifier		Sep	1976	19	
Synthesiser, Transcendent 2000 part 2	Aug	1978	45	Two metre VMOS power amplifier		Feb	1980	27	
Temperature stabilising log converter	Jan	1979	62	Versatile grid dip oscillator		Aug	1975	34	
Touch organ	Dec	1976	41	<b>ROBOTICS</b>					
Transcendent DPX string synthesiser part 1	Aug	1979	18						
Transcendent DPX string synthesiser part 2	Sep	1979	62			Digital PWM interface for the robot motor controller	Jun	1982	66
Transcendent DPX string synthesiser part 3	Oct	1979	35			ETI Mobile 2 robot part 1	Aug	1982	82
Transcendent DPX string synthesiser part 4	Nov	1979	64			ETI mobile 2 robot part 2	Sep	1982	25
Transcendent Poly Synth part 1	Dec	1980	87			Motor Interface	Jul	1986	34
Transcendent Poly Synth part 2	Jan	1981	77			Motor speed control for robots	Jul	1982	59
Transcendent Poly Synth part 3	Feb	1981	32			Proximity detector	Jun	1982	69
Transcendent Poly Synth part 4	Mar	1981	27						
Tuning fork	Feb	1980	79						
Twonky-MPU musical box	Feb	1979	79						
Victory organ part 1	Feb	1983	19						
Victory organ part 2	Mar	1983	36						
Victory organ part 3	Apr	1983	56						
Victory organ part 4	May	1983	67						
Vocoder part 1	Sep	1980	58						
Vocoder part 2	Oct	1980	40						
Vocoder errata	Apr	1981	8						
Voltage controlled digital oscillator	Mar	1985	16						
Voltage controlled digital oscillator errata	Jul	1985	27						
Waa-phase unit	Jun	1981	24						
Waa-Waa unit	Jun	1976	16						
Waveform multiplier (chorus)	Jan	1983	71						

## BIO-FEEDBACK ACCESSORIES



**A METER MOVEMENT** which can be built into your bio-feedback monitor to make it a completely self-contained instrument. Don't worry if you've already drilled the terminal holes - the meter will cover them up!

**SENSITIVE METER MOVEMENT** ONLY £1.90!

**SPARE ELECTRODES AND GEL**

5 sets of electrodes (10 electrode pads) and a sachet of conductive gel, all for £2.90.

## LEDs

**RECTANGULAR LEDs**

Green rectangular LEDs for bar-graph displays.  
50 for £3.50    100 for £6    500 for £25

**DIGITAL AND AUDIO EQUIPMENT LEDs**

Assorted 3mm LEDs: red, green, yellow and orange. 25 of each (100 LEDs) for £8.80

## PROJECT BOX

**WITH BATTERY COMPARTMENT**



As used in our tachometer and bio-feedback kits. This attractive and versatile case can be used to house the experimenter kit projects, or your own battery operated projects.

**PROJECT CASE WITH PP3 BATTERY COMPARTMENT ONLY £2.60!**

## LEDSCOPE

FEATURED IN ETI JANUARY 1987

Tony Ellis's famous LED oscilloscope. The most important bench instrument for any electronics enthusiast must be a 'scope', and at this price anybody can afford one! The Ledscope also acts as a voltmeter and ohm-meter. It's got everything!

The complete parts set includes a smart brushed aluminium case, PCB, all components, pots, knobs, switches, and full instructions.

**LEDSCOPE PARTS SET, WITH CASE ONLY £59.95!**

**SUITABLE PROBE SET £7.95**

## BIO-FEEDBACK

FEATURED IN ETI DECEMBER 1986

A complete parts set for the ETI bio-feedback monitor. Previously offered at £14.55, the last few sets to clear at **£9.99!** We will also supply a free meter movement for the monitor. The complete parts set includes case, PCB, all components, meter and full instructions.



**YOUR LAST CHANCE**

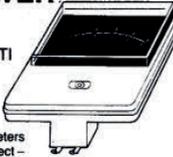
**BIO-FEEDBACK PARTS SET ONLY £9.99!**

**£14.55**  
ONLY UNTIL APRIL 30th  
**WITH FREE METER!**

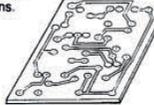
## HI-FI POWER METER

FEATURED IN ETI MAY 1987

Measure the output power of your hi-fi with the ETI power meter. The meters can be back-lit for effect - the scale and 'power' legend will glow green to contrast with the red pointer. Two switched ranges give readings of 0-10W and 0-100W.



The parts set consists of meter movement, PCB, all components, range switch and full instructions.



**MONO POWER METER PARTS SET £3.90**  
**STEREO POWER METER PARTS SET £7.20**  
**SUITABLE CASE £7.50**

## TACHOMETER AND DWELL METER

FEATURED IN ETI JANUARY 1987

**MOTORISTS QUIZ**  
You are driving along the road one day when the sound of a horn makes you look behind. The driver of a milk float is cursing you for driving so slowly. A while later, an invalid carriage overtakes you, and just as you turn into your drive you hear a tractor driver mutter 'At last! I can get out of first gear!'

Do you:

- Fit a £500 Pie-in-ear in-car stereo with digital flexi-woofers and 24-band ramification?
- Buy a set of fluffly dice and sticker saying 'My other car' is a Macaroni?
- Give your car in part exchange for a milk float/invalid carriage/tractor?
- Tune your engine.

The combined tachometer and dwell meter parts set contains: case with battery compartments; printed circuit board; all components; switches; plug, socket and test leads; battery connector; full instructions. The answer to the quiz, by the way, is: a) Buy a bright red Lotus Esprit.

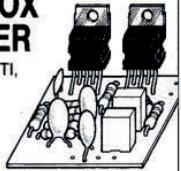
**TACHOMETER AND DWELL METER PARTS SET £12.90** (with terminals for external meter)  
**£16.40** (with self contained meter)

## MATCHBOX AMPLIFIER

FEATURED IN ETI, APRIL 1986

No ordinary amplifiers, these. When our first customers took an interest, it was for the diminutive size (both modules will fit in a matchbox!), the total disregard for power supplies and speaker impedances, and the impressive power output from these little amplifiers. When they re-ordered, it was for the sound quality.

Two amplifier modules were described, both based on the powerful L165V IC. The single IC version will deliver over 20 Watts with a suitable speaker and power supply. The bridge version can provide up to 50W! Although the specified supply voltage and speaker impedance must be used to achieve maximum power, both modules are quite happy to work from any voltage between 12V and 32V, and will accommodate any type of speaker. The bridge version is ideal for giving a boost to car Hi-Fi systems, driving two 4 Ohm speakers in parallel on each channel for best effect. Both designer-approved parts sets consist of a roller tinned printed circuit board and all components. The L165V ICs are also available individually, with a free mini data sheet giving specifications and suggested circuits.



**SINGLE IC MATCHBOX AMPLIFIER SET (20W into 4 Ohms) £6.50**    **BRIDGE AMPLIFIER SET (50W into 8 Ohms) £8.90**    **L165V IC, with data, £3.90**

# Complete Parts Sets for ETI Projects

## MAINS CONDITIONER

FEATURED IN ETI, SEPTEMBER 1986

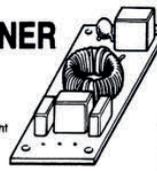
It is astonishing how many people buy or build top-flight hi-fi equipment, and then connect it to a noisy, spiky mains supply. Rather like buying a Ferrari and trying to run it on paraffin, you might think. Expecting crystal clear sound, the poor music enthusiast ends up with a muddy, confused mush, and feels that he has somehow been cheated. 'Is this hi-fi? My music centre sounded just as good!'

The domestic mains supply is riddled with RF interference, noise, transient spikes, and goodness knows what else. Computers crash, radios pop and crackle, tape recordings are spoiled and hi-fi sounds 'not quite right. Why put up with it when the solution is so simple? The ETI mains conditioner is the lowest cost upgrade you will ever buy, and probably the most effective!

Our approved parts set consists of PCB, all components, toroid, enamelled wire, fixing ties, fast response VDR, and full instructions.

**ETI MAINS CONDITIONER PARTS SET ONLY £4.80!**

\*Note: the toroid and VDR supplied are superior to the types specified in the article.



## CREDIT CARD CASINO

FEATURED IN ETI, MARCH 1987

This wicked little pocket gambling machine measures only 3"x2"x1/2". It will play all kinds of casino games, including:

- Roulette
- Craps
- Pontoon

Our approved parts set comes complete with case; self-adhesive fascia; tinned and drilled printed circuit board; all components; hardware; full instructions and three different games to play!

**CASINO PARTS SET ONLY £5.90!**



**SPECIAL OFFER**  
Five extra games FREE with all orders received before April 30th

## MAINS CONTROLLER

FEATURED IN ETI, JANUARY 1987

Have you ever wondered what people do with all those computer interfaces? Put your computer in control, say the ads. 'The Spectrabeeb has eight TTL outputs. What on earth can you control with a TTL output? A torch bulb?'

The ETI Mains Controller is a logic to mains interface which allows you to control loads of up to 500W from your computer or logic circuits. An opto-coupler gives isolation of at least 2,500V, so the controller can be connected to experimental circuits, computers and control projects in complete safety. Follow your computer interface with a mains controller and you're really in business with automatic control!

The mains controller connects directly to most TTL families without external components, and can be driven by CMOS with the addition of a transistor and two resistors (supplied).

Your mains controller parts set contains: high quality roller tinned PCB; MOC3021 opto-coupler; power triac with heatsink, mounting hardware and heatsink compound; all components, including snubber components for switching inductive loads; transistor and resistors for CMOS interface; full instructions.

**MAINS CONTROLLER PARTS SET £6.20**



## POWERFUL AIR IONISER

FEATURED IN ETI, JULY 1986

Ions have been described as 'vitamins of the air' by the health magazines, and have been credited with everything from curing hay fever and asthma to improving concentration and putting an end to insomnia. Although some of the claims may be exaggerated, there is no doubt that ionised air is much cleaner and purer, and seems much more invigorating than 'dead' air.

The DIRECT ION ioniser caused a great deal of excitement when it appeared as a constructional project in ETI. At last, an ioniser that was comparable with (better than?) commercial products, was reliable, good to build... and fun! Apart from the serious applications, some of the suggested experiments were outrageous!

We can supply a matched set of parts, fully approved by the designer, to build this unique project. The set includes a roller tinned printed circuit board, 66 components, case, mains lead, and even the parts for the tester. According to one customer, the set costs about a third of the price of the individual components. What more can we say?

**DIRECT ION PARTS SET £9.50**



## MATCH BOX AMPLIFIERS

**20W Single IC parts set £6.50**

**50W Bridge Amplifier parts set £8.90**

**L165V Power Amplifier IC, with data, £3.90**

## LM2917 EXPERIMENTER SET

Consists of LM2917 IC, special printed circuit board and detailed instructions with data and circuits for eight different projects to build. Can be used to experiment with the circuits in the 'Next Great Little IC' feature (ETI, December 1986).

**LM2917 Experimenter Set £5.80**

## RUGGED PLASTIC CASE,

suitable for mains controller and mains controller.

**ONLY £1.65**



## WHITE IONISER PARTS SET ONLY £9.80!

Our best selling ioniser kit is now available with an elegant white case.

**WHITE IONISER PARTS SET ONLY £9.80!**

Orders should be sent to Specialist Semiconductors at the address below including 80p towards postage and packing. Please allow up to 14 days for delivery. There is no telephone service at the moment, but all letters or requests for lists will be answered (at top speed if you send SAE!)

**Specialist SEMICONDUCTORS**  
FOUNDERS HOUSE REDBROOK MONMOUTH GWENT

# MIDI MASTER KEYBOARD

PROJECT

John Yau continues his MIDI keyboard with a description of the all-important CPU board and the front panel.

Having put the keyboard together, the major part of the MIDI Master Keyboard should be assembled — the controlling CPU and its associated electronics.

The CPU is a 6502A microprocessor and it looks after the entire keyboard (Fig. 1). The majority of the circuitry is on two boards — the CPU board and the Front Panel board. The latter is largely a base for all the front panel switches and displays. The CPU board is the most complex board and is a double sided PCB.

The MIDI Master Keyboard is implemented in a simple 6502 memory map (Fig. 2). All the interfaces for the keyboard itself, the front panel, the MIDI interfaces and so on are mapped into specific location in the memory map and the whole system controlled by a monitor program in ROM.

## Construction

The CPU board is the most complex board as far as

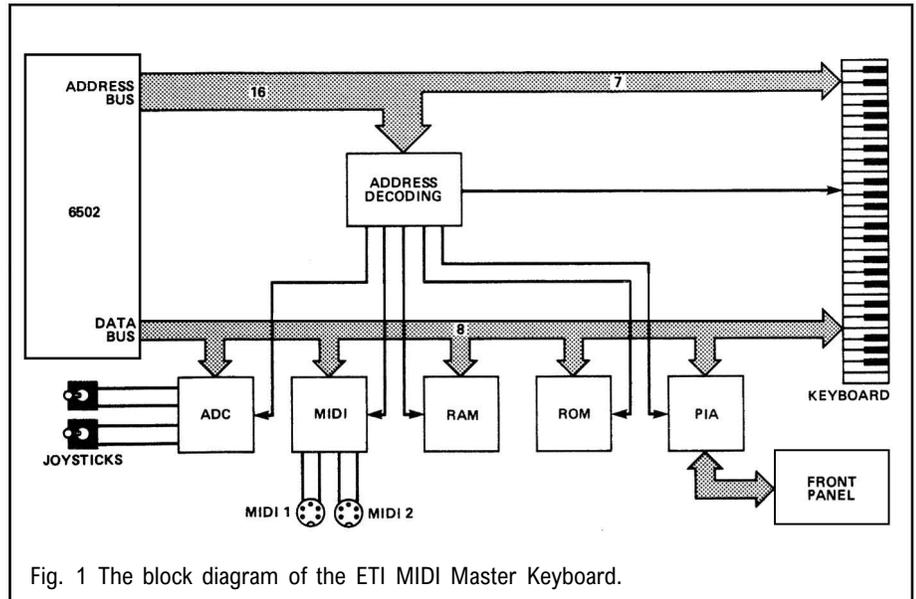


Fig. 1 The block diagram of the ETI MIDI Master Keyboard.

component count is concerned and with the added fact that it is double sided, it demands much care and attention if it is to be assembled correctly.

The first task is to insert and

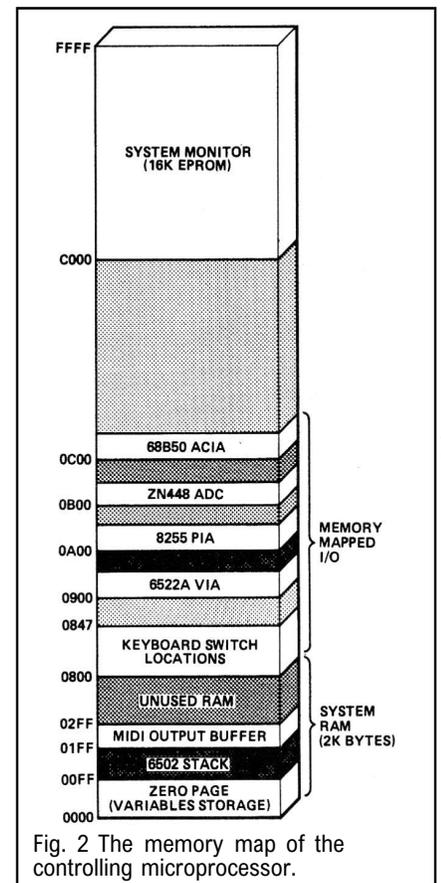
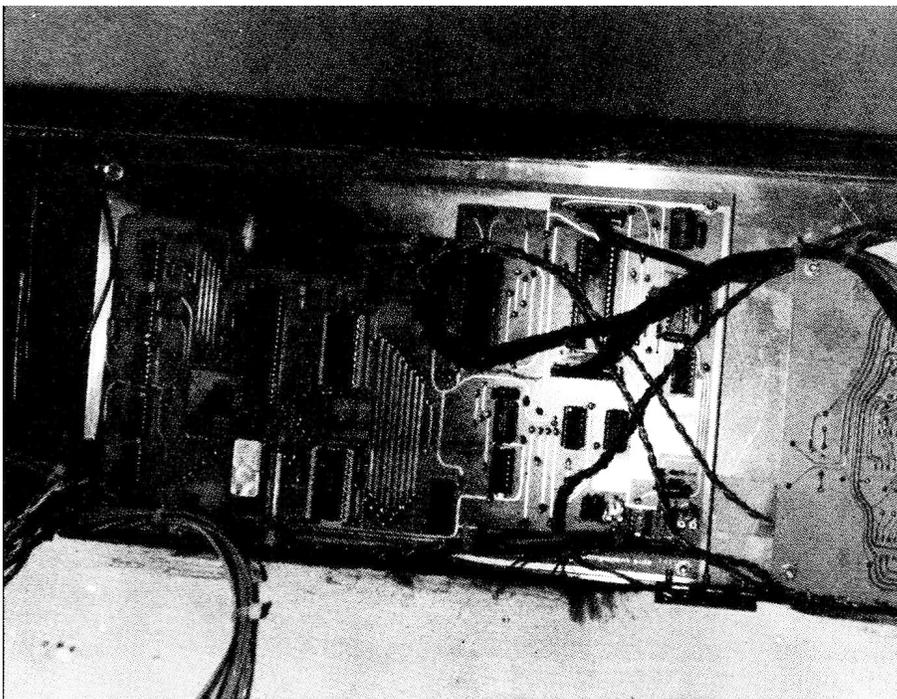


Fig. 2 The memory map of the controlling microprocessor.



# PROJECT

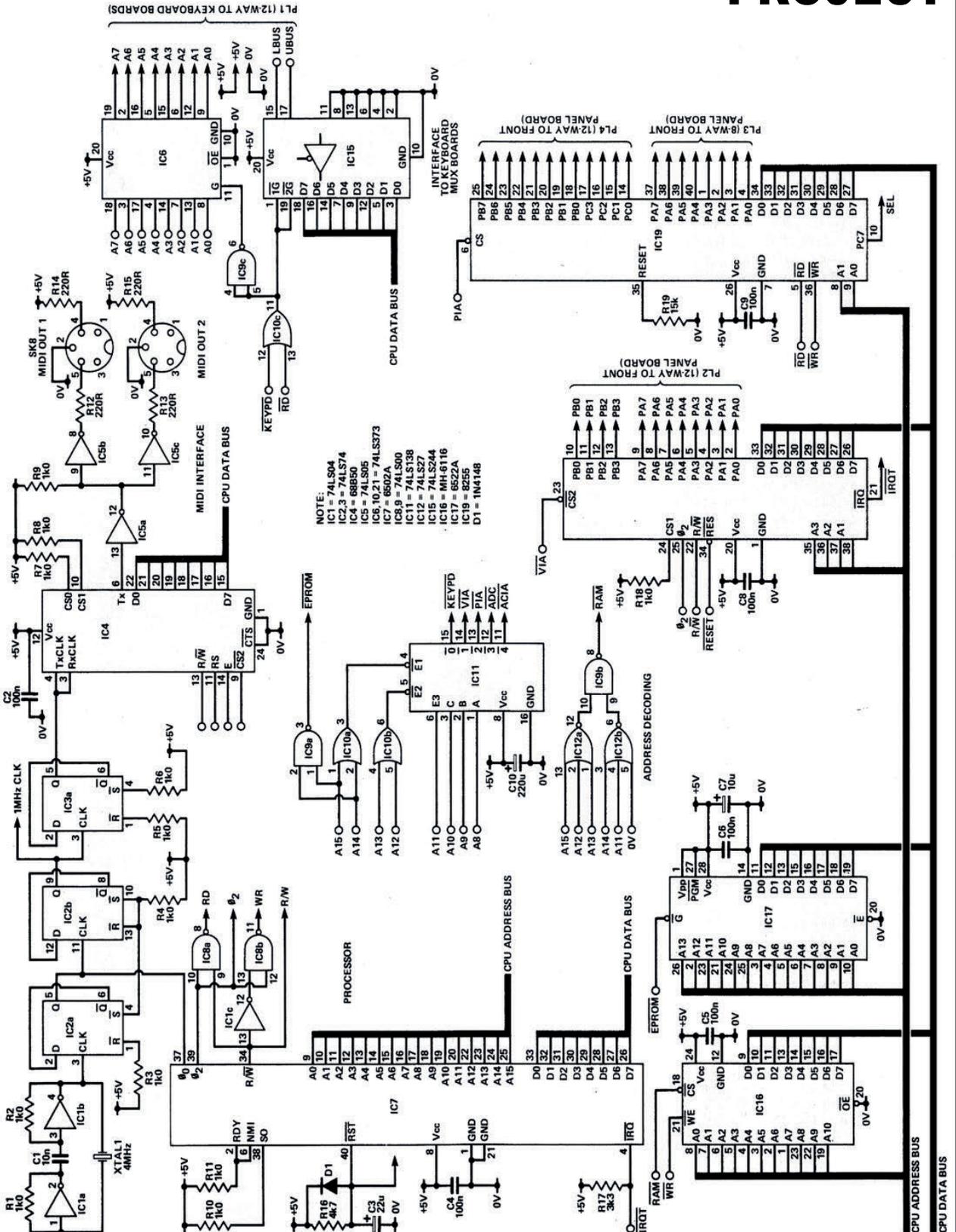


Fig. 3 The circuit diagram of the CPU board.

## HOW IT WORKS - CPU

Figure 3 shows the circuit diagram for the CPU board. C3, R16 and D1 form a simple power up reset circuit that is used by the 6502A and also the 6522A VIA. IC1a and IC1b form a 4MHz crystal oscillator. IC2a divides the latter signal by two to form the 2MHz clock for the 6502A. Further division of the 2MHz clock signal is performed by flip flops IC2b and IC3a to obtain the 31.125kHz clock signal used by IC4, the 68B50 ACIA.

Address decoding for the CPU is performed by IC9, IC10, IC11 and IC12. The address decoding enables all the peripheral devices to be memory mapped within the 6502A's address space.

The monitor program for the processor resides permanently in EPROM, the device used being a 16K 27128 EPROM (IC17). A 6116 2K CMOS RAM chip provides the required RAM workspace. Since the size of the monitor program is only about 2.5K of 6502 code, using a 16K EPROM may seem a bit of an overkill. However, the larger EPROM was chosen to give scope for expansion (such as storage of voice dumps for particular synthesisers) and also because of the relatively small price difference when compared to smaller devices.

### 6522A VIA Functions

IC18 is a 2MHz version of the 6522 Versatile Interface Adaptor (VIA), the 6522A. The device takes up 16 locations in the 6502's memory address space and these are accessed when using the device's dual 8-bit ports and on-board timer. The 6522A is configured to perform two functions.

Scanning of the data entry and function push button key-pad is achieved by the two I/O ports. The 6522A's timer is responsible for generating the clock signal which interrupts the 6502A processor every 2ms. Virtually all the system software is interrupt driven, due to the demands of scanning the keyboard at the precise time intervals required for the key velocity sensing.

### 8255 PIA Functions

IC19 is an 8255 Peripheral Interface Adaptor (PIA) interfaced to the 6502A through four memory mapped locations. These addresses are the 8255's three 8 bit I/O ports and its control register.

The RD and WR signals for the device are derived from the 6502A's Phi-2 clock and R/W lines using IC1c, IC8a and IC8b. In use, the PIA is configured simply as three 8 bit output ports which are used to drive the LED displays of the MIDI keyboard.

### The Keyboard

The multiplexer circuitry for the key scan hardware was described last month. In order to maximise speed and efficiency in the key scanning each key address is made to appear as a direct memory location in the 6502's address space (from 0800H to 0847H). The timing diagram for accessing the state of each key is shown in Fig. 5.

Two successive memory read cycles are required, the first being a dummy read that causes the address of the key to be latched at IC6, a 74LS373 octal latch. As there are only 72 keys to be addressed the most significant bit of the latched address will always be zero.

By the time the following read cycle occurs the two bit word describing the state of the key will be valid at the inputs of IC15, a 74LS244 tri-state octal latch whose output is connected to the processor data bus. It is necessary to latch the key address rather than to engage in a single read cycle because the CMOS multiplexer device outputs are unable to settle within the maximum 310ns access time of a single 6502A read cycle.

### The MIDI Interface

Transmission of MIDI messages is achieved by IC4, a 68B50 Asynchronous Communications Interface Adaptor (ACIA). Note the device has to be a 'B' version in order to be compatible with the 2MHz 6502A. Only two memory-mapped locations are required for full communication with the device.

When a single byte of MIDI data is to be transmitted it is simply written to the 68B50's transmit data register by the 6502 processor. The 6502 can then resume its other tasks whilst the ACIA has the job of converting the parallel data to a serial output of one start bit, eight data bits and one stop bit at a baud rate of 31.125K — the standard MIDI data configuration.

Inverters IC5a, b and c are of the open collector type and are used to form the current loop required for the serial link with an external MIDI device. Both MIDI OUTs are identical, the dual output may be useful in avoiding having a large number of MIDI devices being daisy-chained from a single MIDI OUT. Using two MIDI OUTs in a star configuration, as was shown last month, greatly reduces the inherent delays in MIDI data propagating itself through the MIDI devices.

The receiver part of the ACIA is not used, since the keyboard does not make any use of the received MIDI data.



with solder when mounting the IC sockets.

Next, solder in the multi-way connectors. Ensure their orientation is correct and keep the contact with the soldering iron to a minimum, so as not to soften the plastic and bend the pins.

The other components can then be mounted, starting off with the resistors, followed by the capacitors, diode and presets. Make sure that the orientation is correct for the electrolytics and diode. Note that a few of the components require their leads to be soldered to the PCB on *both* sides.

Finally, insert all the integrated circuits and, as always, ensure correct orientation. Finish off by cleaning the board with flux remover and check thoroughly for any shorts which may be caused by stray blobs of solder.

### Front Panel Board Assembly

The front panel PCB holds the display driver and display circuitry as well as functioning as a mounting base for the bank of push buttons.

First of all, solder in the links as shown in the layout diagram (Fig. 7). Follow this with the resistors, diodes and IC sockets, making sure the diodes are correctly orientated.

The dual 7 segment display plugs into a 24 pin DIL IC socket mounted on the PCB. Since the display device package only has 18 pins be sure that it is plugged into the socket correctly. It should occupy the leftmost position when the PCB is viewed from the component side.

The next components to be added should be the push buttons. To achieve best alignment

solder all the through-pins. Refer to the component layout diagram (Fig. 6) and use double sided veropins. Make sure that *both* sides are soldered. Making doubly sure that the through-pins are correctly soldered will save a lot of time and frustration later on. It

only takes one side of a through-pin to be overlooked for the board to malfunction.

Solder in all the IC sockets next. Some of the tracks between the IC pins on the PCB are rather fine, so be careful not to accidentally bridge any of them

# PROJECT



## HOW IT WORKS FRONT PANEL

Figure 4 shows the circuit of the front panel board and the joystick control section of the CPU board.

Scanning of the push button key-pad is achieved by the diode matrix circuit comprising D2-30, SW1-29 and R57-64. Port A of the 6522A VIA is configured to be an input port, and the low nibble of port B is configured for output. By reading the value of the data presented at port A, whilst one of the switch matrix rows is pulled low (strobed) by the relevant bit in port B, the state of all the switches in that row can be examined.

For example, if the binary number 1111101 was placed in port B, the second row of the switch matrix strobed and the value of data from port A were say 1110111, then it can be deduced that the numeric button '4' was being pressed.

Such circuits are commonly found in 'QWERTY' keyboards, but there are problems using this type of circuit for scanning the music keyboard as well. Full polyphonic scanning of the keyboard is awkward to achieve and the large number of diodes required would be undesirable.

The 8255 PIA on the CPU board drives the LED displays on the front panel. Port A data goes to the two 74LS47 seven segment display driver devices (IC22 and 23) on the front panel PCB, which in turn drives the dual digit display on the same board. Ports B and C drive the single LED displays via inverter buffers IC24 and 25, a pair of 7405s. To light up a LED, logic one has to appear at the relevant bit. The inverter then sinks the current required to illuminate the LED.

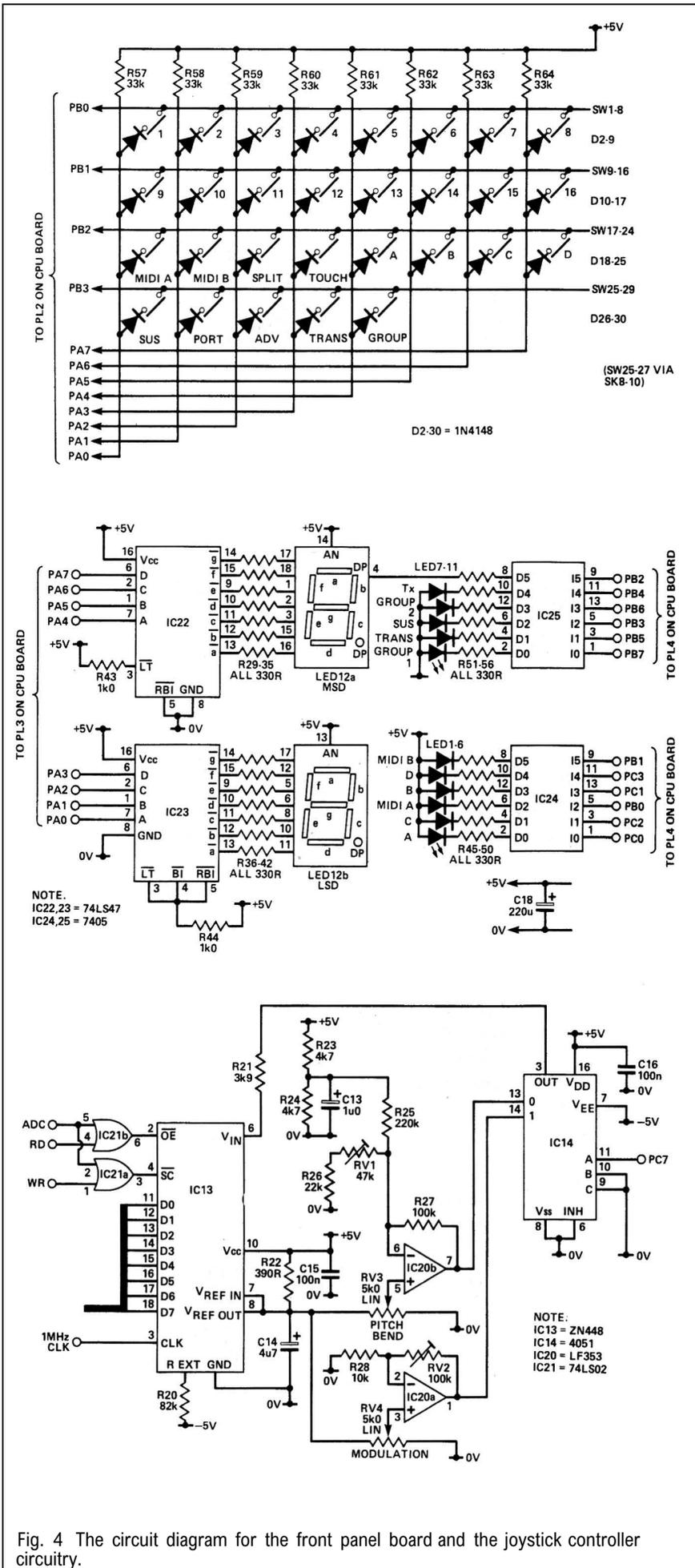


Fig. 4 The circuit diagram for the front panel board and the joystick controller circuitry.

## HOW IT WORKS - JOYSTICKS

### Joystick Interface

The joystick interface has the task of enabling the 6502A processor to digitally read the positions of two joysticks. Both mechanical assemblies of the joysticks have 5k linear rotary potentiometers coupled to the joystick lever pivot points. The joystick assembly intended for the pitch bend has a self centering lever whilst the modulation joystick is of the ratchet type.

Since the full travel of the joystick assembly is only about 20% of the full potentiometer track there are added complications if we are to ensure that the maximum deviation of the joystick position will correspond to the maximum digitised value of 255 from IC13 (a ZN448 8-bit A/D converter).

The ZN448 is configured to use its own internal voltage reference of 2.5V. This voltage reference is also fed to the top end of the joystick potentiometer tracks. If the minimum joystick deviation corresponds to an output of 0V at the wiper then at the other extreme position the output voltage will be approximately 20% of the reference voltage — about 0.5V.

To utilise the full dynamic range of the A/D converter an input voltage of 2.5V is required when the joystick is at full travel. This is achieved by amplifying the wiper voltages before they are presented to the input of the A/D converter. IC20a and IC20b form two non-inverting voltage amplifiers with gains that can be fine adjusted by preset trimmers RV1 and RV2.

When the pitch bend joystick potentiometer on the prototype master keyboard was set to give a 0-0.5V range at the wiper it was found the neutral position did not correspond to the expected voltage of 0.25V, resulting in a slightly asymmetric deviation of voltages when moved from the centre to the extremes of travel. This is because

the potentiometer track is not completely linear throughout the whole of its span. In order to minimise this non-linearity it was necessary to move the working part of the potentiometer track to roughly its middle region. In such a set-up the wiper voltage is in the range 1.0-1.5V when the joystick is at its lowest extreme of travel. The latter displacement voltage must be cancelled out so that the correct range of 0-2.5V appears at the A/D converter input. This is achieved by imposing a DC offset at pin 6 of IC20b, resulting in a voltage subtraction of approximately 1.2V at the output of the op-amp.

IC14 is a 4051 used as a two input analogue multiplexer. PC7 from IC19, the 8255 PIA, selects one of the two joystick voltages to be presented to the input of the A/D converter (pin 6). The A/D converter appears to the 6502A processor simply as a single memory mapped location (0B00H). Writing to 0B00H initiates a conversion start and after the conversion time span has elapsed (approx. 10us) the data can be read from the same location.

For a given joystick position the data read from the A/D converter should always be exactly the same in the ideal case. This would allow the software to transmit the relevant MIDI information only when the joystick position has just changed. However, in reality the least significant bit can fluctuate in successive readings for certain joystick positions due to the limited resolution of the A/D converter. A solution to this problem is to collect successive sample readings and take the average, thereby greatly reducing any occasional perturbations in the data. The software fix was found to be quite effective, although it effectively resulted in a reduction in the rate at which the joystick positions were scanned.

of the push button bank, the switches should be soldered to the PCB fully assembled, complete with the key cap tops. Solder the push buttons one by one, making sure the positioning is straight and square.

There are three wiring harnesses which span from the front panel board to the CPU PCB. Each harness should be soldered directly onto the relevant pins and terminated with a female multi-way PCB connector. As with the keyswitch PCBs, the wiring has to be directly soldered onto the front panel PCB (rather than using multi-way connectors) due to lack of clearance when the board is mounted in position in the keyboard cabinet.

Follow the component layout diagrams of both the front panel board and the CPU board to ensure correct connector orientation. Cable length should be such that the wiring reaches the CPU board easily from the front panel board when the two boards are in their final mounting positions within the keyboard cabinet.

After plugging in the ICs, all that remains is the wiring of the two harnesses for the LEDs. Wiring should be direct to the board or via veropins. Be careful with the LEDs' orientation as it's very easy to get one of them wrong (see Fig. 7). Use solid insulated wire for the anode connection to give the LEDs a more definite mounting base and position the LEDs with the final front panel positions in mind (see Fig. 9).

That completes the construction of the CPU and front panel boards. Next month we shall look at the power supply board and wire up all the boards together. We shall also see what kind of cabinet is best suited to the MIDI Master Keyboard.

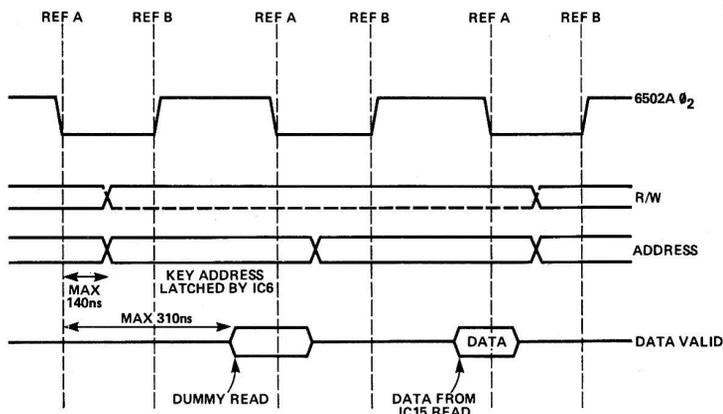


Fig. 5 Timing diagram for the keyboard scan.



# PROJECT

## PARTS LIST CPU BOARD

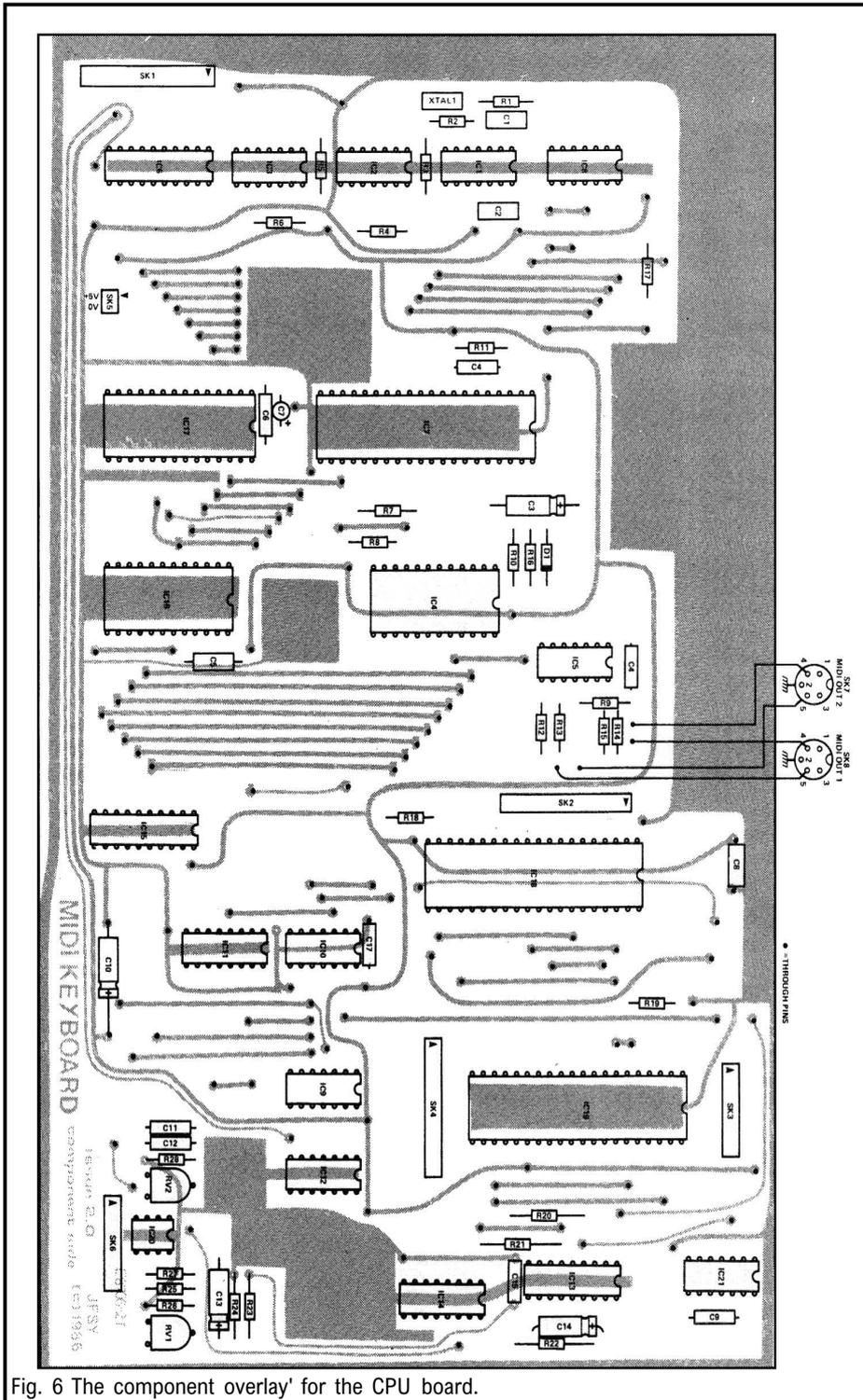


Fig. 6 The component overlay for the CPU board.

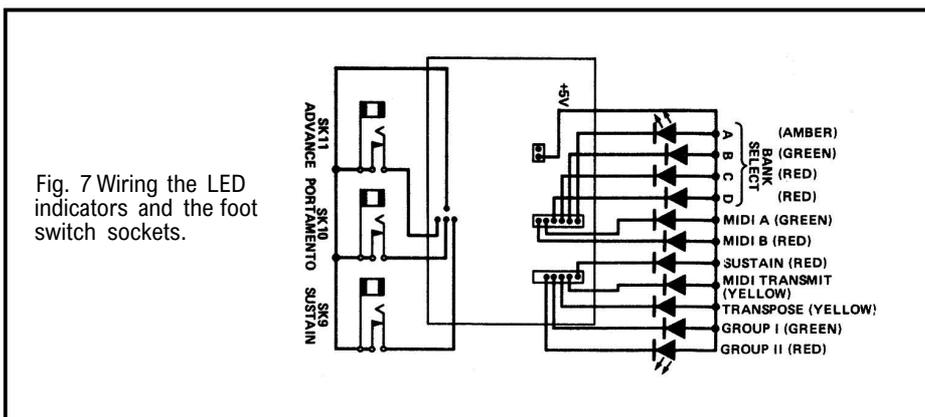


Fig. 7 Wiring the LED indicators and the foot switch sockets.

### RESISTORS

R1-11, 18	1k0
R12-15	220R
R16, 23, 24	4k7
R17	3k3
R19	15k
R20	82k
R21	3k9
R22	390R
R25	220k
R26	22k
R27	100k
R28	10k
RV1	47k horiz. preset
RV2	100k horiz. preset
RV3	5k0 lin. single axis joystick (centre sprung)
RV4	5k0 log single axis joystick (ratchet)

### CAPACITORS

C1	10n polycarbonate
C2, 4, 5, 6, 8, 9, 11, 12, 15, 16, 17	100n polyester
C3	22u 16V electrolytic
C7	10u 16V tantalum
C10	220u 16V electrolytic
C13	1u0 16V electrolytic
C14	4u7 16V electrolytic

### SEMICONDUCTORS

IC1	74LS04
IC2, 3	74LS74
IC4	68B50
IC5	74LS05
IC6, 10, 21	74LS373
IC7	6502A
IC8, 9	74LS00
IC11	74LS138
IC12	74LS27
IC13	ZN448
IC14	4051
IC15	74LS244
IC16	HM-6116
IC17	27128
IC18	6522A
IC19	8255
IC20	LF353
IC21	74LS02
D1	In4148

### MISCELLANEOUS

SK1, 2, 4	12-way PCB connector
SK8, 6	8-way PCB connector
SK5	2-way PCB connector
SK7, 8	5 pin DIN
XTL1	4MHz crystal
PCB; IC sockets; nuts and bolts.	

### BUYLINES

The joysticks used were from SLM. (Modes) Ltd., Chiltern Road, Prestbury, Cheltenham, GL52 5JQ. The other components should pose few problems. The PCB is available from our PCB, Service.

# PROJECT

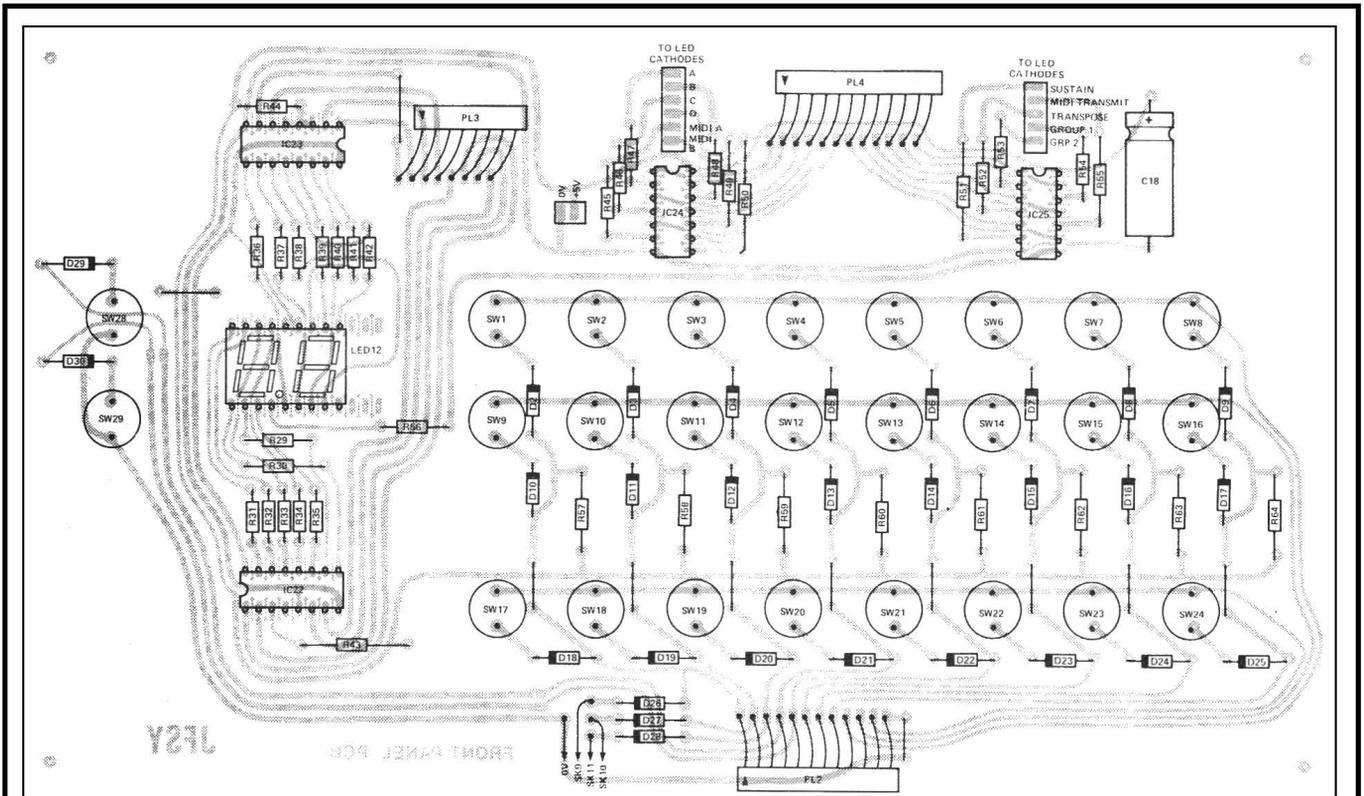


Fig. 8 The component overlay for the front panel board.

## PARTS LIST - FRONT PANEL

<b>RESISTORS</b>		<b>LED8, 11</b>	<b>Yellow LED</b>
R29-42, 45-56	330R	<b>LED12</b>	<b>Double digit 7 segment display (common cathode)</b>
R43, 44	1k0		
R57-64	33k		
<b>CAPACITORS</b>		<b>MISCELLANEOUS</b>	
C18	220u 16V electrolytic	PL2,4	12 way PCB connector
<b>SEMICONDUCTORS</b>		PL3	8 way PCB connector
IC22, 23	74LS47	SW1-24, 28, 29	Push button switch
IC24, 25	7405	SW25-28	Foot switch
D2-30	1N4148	SK9-11	¼in jack socket
LED1	Amber LED	PCB; IC sockets; PCB through pins; nuts and bolts.	
LED2, 5-7, 9	Red LED		
LED3, 4, 10	Green LED		

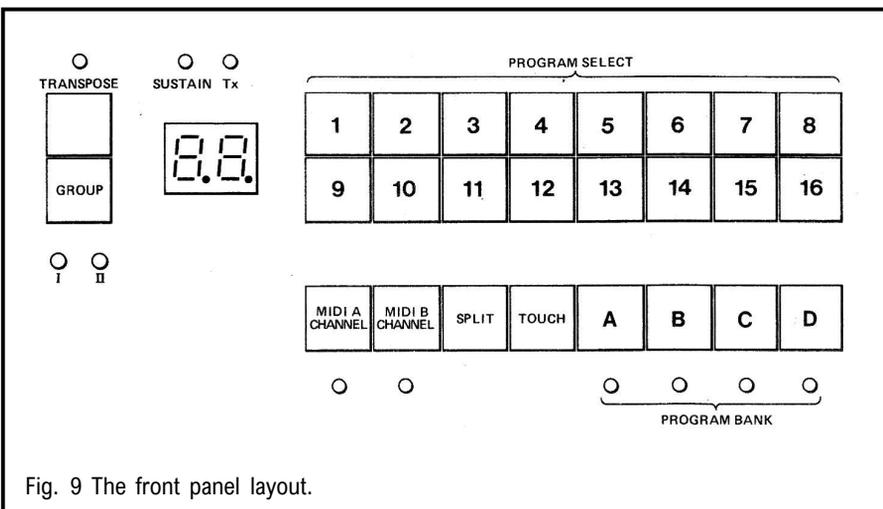


Fig. 9 The front panel layout.

# FLAME SIMULATOR

Pretend arsonist Gary Hynes puts realism into electric fires, candle bulbs, and other pseudo-flames with this ingenious device.

There are many household appliances which require a simulated flickering flame. 'Olde' pseudo-candle lights (such as 'carriage' lamps) and many electric fires simulate flames either with bulbs using thermal cutout filaments (effectively glass-encapsulated car flasher units!) or by mechanical means consisting of complicated motorised reflectors.

The problems with both of the methods are twofold. First, these methods of flame simulation are unreliable. The mechanical means often jam and the reflectors soon lose their gleam inside an electric fire. The flicker filaments soon over-flick and die.

These flame simulators also suffer from a severe lack of realism! Both produce a pretty regular flicker — quite unlike a real flame.

This device is the all-electronic solution to these problems. The unit uses an ordinary mains bulb of 60W or less and flickers it in an apparently totally random manner. In between the flickers the bulb is still lit dimly and this also helps to more realistically imitate a flame's light dance.

## Operation

A simplified block diagram of the circuit is shown in Fig. 1. The circuit is based around a pseudo random sequence generator (PRSG) which generates an apparently random sequence of bits (ones and zeros) at the speed of the clock oscillator.

The sequence is in fact not truly random. It actually follows a continually repeated set pattern. However, if the sequence is made long enough the repetition cannot be noticed and appears as random as a flame.

The PRSG is formed by a 20-stage shift register. Outputs from the 17th and 20th stages are

fed to the inputs of an exclusive OR gate and the output from this is fed back to the input of the first stage.

The feedback connections are critical if the maximum sequence length is to be achieved. This is known as the maximal length.

The calculations for finding the

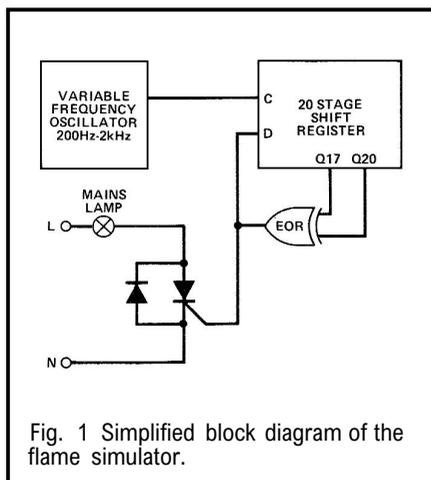


Fig. 1 Simplified block diagram of the flame simulator.

## HOW IT WORKS

The circuit diagram of the flame simulator is shown in Fig. 2. The mains voltage is stepped down by transformer T1 to 6V AC, full wave rectified by diodes D1,2 and smoothed by capacitor C1 to provide a DC supply of about 7V to power the circuit.

Note that the 0V line is connected directly to the neutral of the mains. LED3 is connected across the supply to indicate the unit is on.

The 20 stage shift register is formed by two ICs. IC1 is a 4006 shift register that provides the first 18 stages while IC2 is a 4013 flip flop providing the 19th and 20th stages. The set and reset inputs are disabled by connecting them to 0V.

The outputs from the 17th and 20th are exclusive ORed by IC3a and its output is fed back to the data input of the first stage via coupling capacitor C5.

R7 and C5 prevent the possibility of the PRSG 'hanging up' permanently in the all-zero state. If this happens C5 will begin to charge through R7 until even-

connections necessary for maximal length are complicated and beyond the scope of this article. What's more they are usually avoided anyway, by repetitive interactive calculations giving a look up table.

The output from the EXOR gate is fed to the gate of a thyristor. During the negative half cycle of the mains the thyristor is turned off and the diode conducts, lighting the lamp dimly.

If the thyristor receives a one on its gate from the PRSG during the positive half cycle then it will conduct, lighting the lamp more brightly. When a zero is received the thyristor turns off during the positive half cycle and the lamp remains dimly lit.

The resultant effect is a lamp that flickers in a random manner. The flicker rate may be adjusted to give the most realistic flicker for the application by changing the oscillator frequency clocking the shift register.

ually a logic one is fed to the input of the first stage restarting the sequence.

A variable frequency oscillator, adjustable from 200Hz to 2kHz, is formed by EXOR gates IC3c and IC3d, C34 and RV1 connected in the well known CMOS oscillator configuration. Because IC1 is clocked on a negative edge and IC2 on a positive edge the clock to IC1 has to be inverted by IC3b.

The output from IC3a is a random sequence of high and low logic levels. These are fed to the gate of thyristor SCR1 via R34. In between 'on' flickers the lamp is kept glowing dimly by diode D4 which conducts during the negative cycle of the mains.

If during the positive cycle the gate of SCR1 receives a high level from the output of IC3a then SCR1 will conduct lighting the lamp brightly.

R2 and C2 form a snubber suppression circuit which controls the maximum rate of change of voltage and the peak voltage across SCR1.

# PROJECT

## Testing

Connect a lamp to the output and the unit to the mains and switch on. If all is well the LED should light and the lamp will begin to flicker.

If this does not happen switch off, unplug the unit from the mains and check for errors. The flicker rate should be adjustable by the preset RV1. This should be adjusted when the unit is unplugged or with an isolated tool (and with care!).

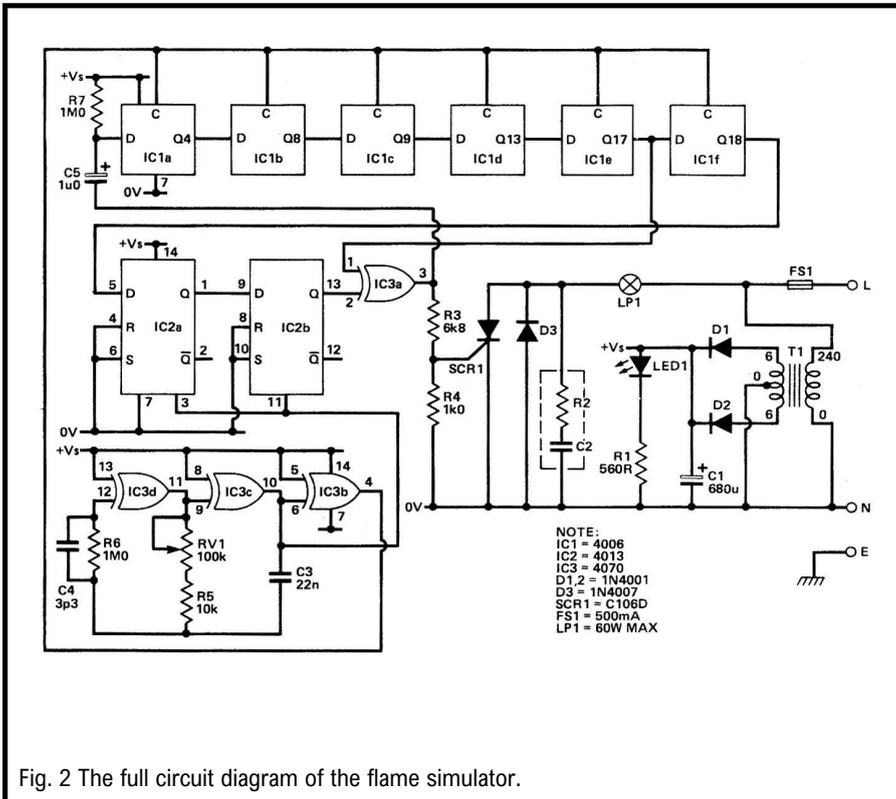
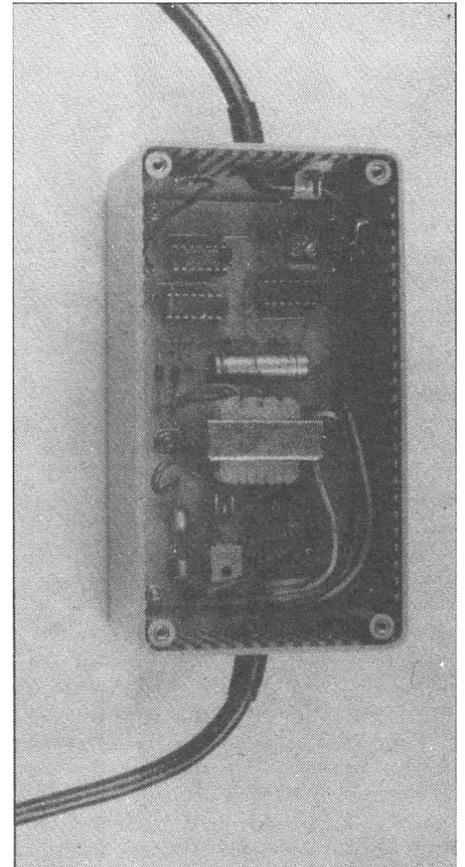


Fig. 2 The full circuit diagram of the flame simulator.

## Construction

The component overlay is shown in Fig. 3. All the components except for the LED are mounted on the single PCB. This is divided by the transformer into two halves — one the mains voltage 240V section and the other the control circuit. However, the entire board is connected directly to the mains input and should not be handled when the unit is plugged in.

Begin by connecting the DIL sockets. Then mount the resistors, capacitors, diodes, the preset, the thyristor, suppressor, transformer

and fuse clips. The ICs should be inserted last of all. As these are CMOS devices, normal anti-static precautions should be observed.

The prototype was mounted in a plastic case measuring 150 x 80 x 50mm. If a metal case is used it must be properly earthed. Care should also be taken to ensure the mains is connected the right way round.

Mains input is from an ordinary three-pin plug and the output is connected to a suitable holder for the lamp to be used. Cables in and out of the unit should pass through grommets.

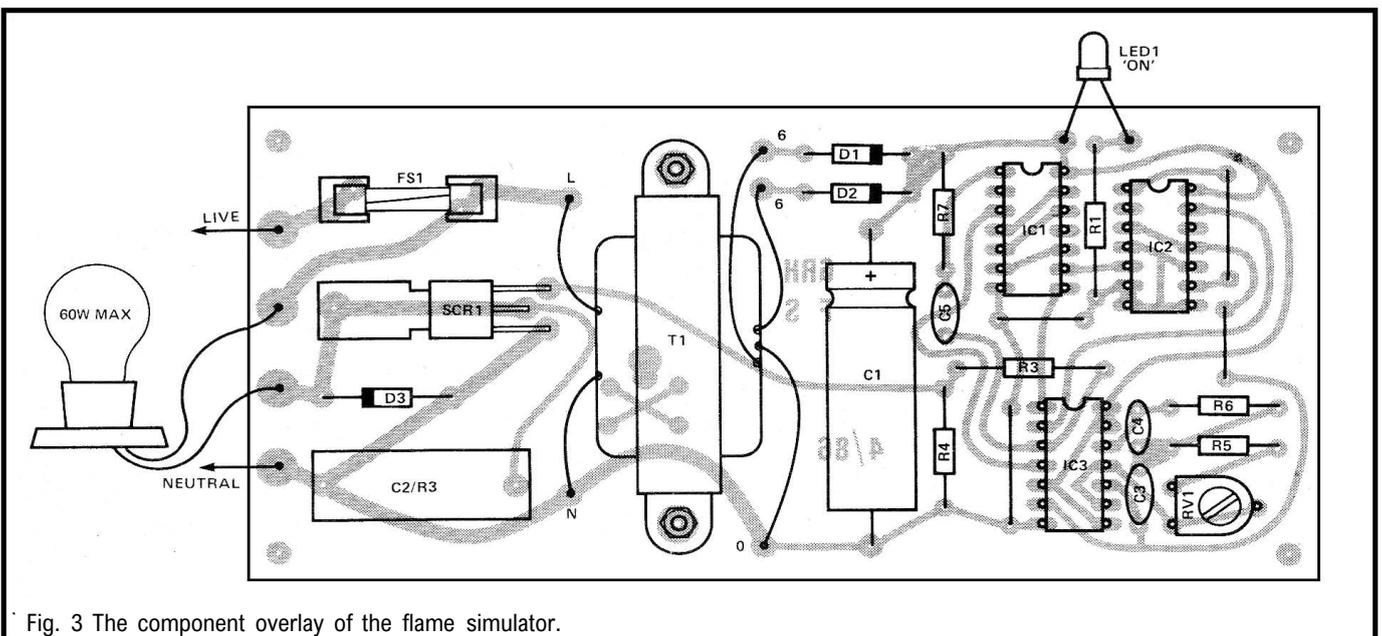


Fig. 3 The component overlay of the flame simulator.

# PROJECT

## PARTS LIST

### RESISTORS all 1/4W, 5%

R1 560R  
 R2 100R (see text)  
 R3 6k8  
 R4 1k0  
 R5 10k  
 R6,7 1M0  
 RV1 100k horizontal preset

### CAPACITORS

C1 680u 16V electrolytic  
 C2 100n (see text)  
 C3 22n polyester  
 C4 3p3 ceramic  
 C5 1u0 16V tantalum

### SEMICONDUCTORS

IC1 4006  
 IC2 4013  
 IC3 4070  
 SCR1 C106D thyristor  
 LED1 Red LED  
 D1,2 1N4001  
 D3 1N4007

### MISCELLANEOUS

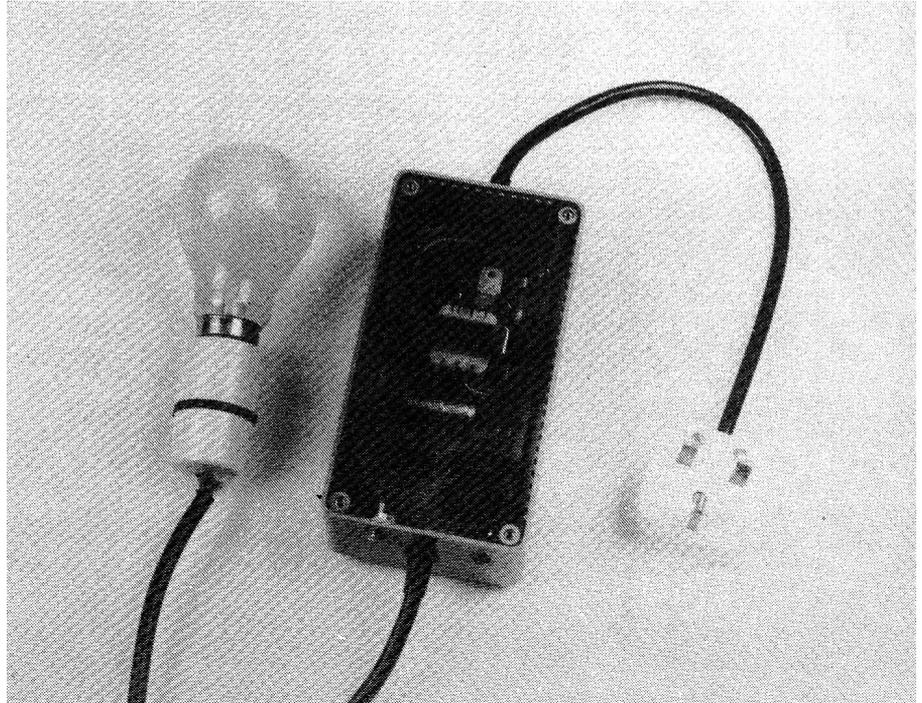
T1 6-0-6V mains transformer  
 C2,R3 contact suppressor

PCB; case; 500mA fuse and fuse clips; IC sockets; 3 amp mains cable; lamp socket.

## BUYLINES

All the components are easily available from the usual suppliers. The case used is not critical and will depend on the application of the circuit.

The mains transformer is available from Maplin (type number WBOOA) as are R2 and C3 - the encapsulated snubber circuit (type number YR90X).



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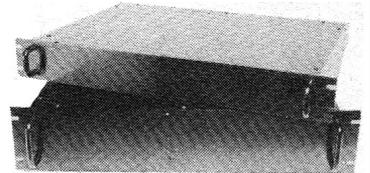
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# HI-FI POWER METER

Paul Chappell builds the ultimate power meter that puts all others to shame and is the definitive upgrade for top-flight Hi-Fi.

Last month I described the three kinds of power associated with electronic circuits — apparent power, real power and reactive power. I also offered a few thoughts on deriving signals to drive the meter without disturbing the signal from the amplifier.

The method eventually chosen was to detect the magnetic flux around one of the speaker leads by means of a ferrite toroid wound with a suitable pickup coil. The result is this month's project — a power meter for top flight hi-fi equipment.

## The Circuit

The final circuit of the power meter is shown in Fig. 1. I say final because it passed through a

## HOW IT WORKS

The amplifier current is sensed by current transformer T1 and the voltage by C4 and C5. The sensing arrangement has a number of advantages. The primary concern is to not disturb the signal from amplifier to speaker in any way. The second is that the power meter should not be influenced by the DC voltage levels of the amplifier output — a failing of most other power meters. The use of a transformer and capacitors gives complete isolation.

The voltage is processed by an instrumentation amplifier consisting of IC3a, b and c. This arrangement gives the same input resistance on each lead, rejects voltages common to both and amplifies the difference.

circuit for best common mode rejection.

The multiplier, IC2, has been described in detail in the text. Its output currents are processed by IC4a to give a single ended voltage output centred on 0V. Power consumed by the load causes the mean voltage level at the output of IC4a to fall, drawing current from RV4 and R26.

This current is applied to the meter via R27, which allows the output of IC4b to operate at a higher voltage level than would be possible if the meter was connected directly across the IC.

In combination with D1, R27 also limits the maximum reverse current that can be applied to the meter under fault conditions.

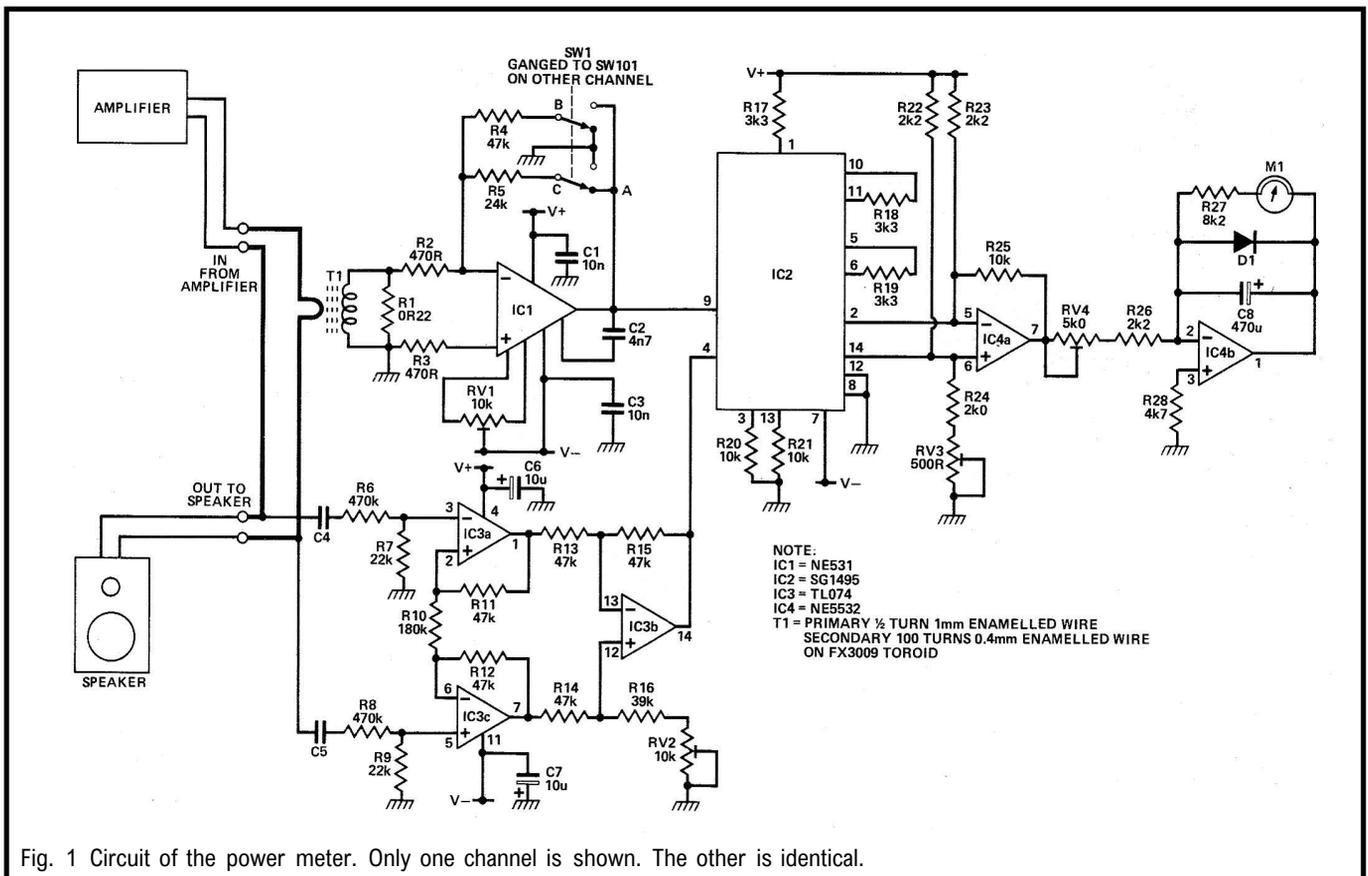


Fig. 1 Circuit of the power meter. Only one channel is shown. The other is identical.

number of stages of development before reaching its present form.

To derive a signal which is a true reflection of the amplifier's current output, the toroid coil must be terminated by an extremely small resistance. Experiment showed that a few ohms would introduce significant phase shift in the current signal. Since a 3° shift between the voltage and current signals will result in a multiplier error of 5%, the phase is quite critical. To meet the performance criteria I set myself for this project, the resistance had to be one ohm or less.

There is no reason why a physical resistor of small value shouldn't be connected across the coil. The current signal can then be detected as a voltage across the resistor and amplified to a usable level. This is the approach taken in the circuit of Fig. 1, and it gives excellent results.

It must be said, however, that this approach is not ideal. As far as the coil is concerned, R1 should be as small as possible but to achieve a good clean signal with the minimum of noise, R1 should be fairly large. This conflict means that the choice of value for R1 is something of a compromise.

An attractive idea would be to feed the coil into some kind of electronic circuit which would maintain both ends of the secondary at the same voltage and sense the current directly. A great deal of effort was expended in trying to achieve this and anyone faced with a similar problem may be interested to know what not to try.

## Current Sauce

Having a requirement for a current amplifier, or a current to voltage converter, of fairly exacting specifications brings home the lack of ICs designed to process currents rather than voltages and the grossly inadequate performance of the few that do exist. It soon became clear that the matching would have to be achieved with the common or garden VCVS op-amps.

A current summing junction can be made without difficulty — Fig. 3a shows the general idea. The positive input of the op-amp is grounded, the negative input is held at 0V by the action of the feedback resistor. The secondary of the transformer 'sees' a short circuit and the output voltage is proportional to the current

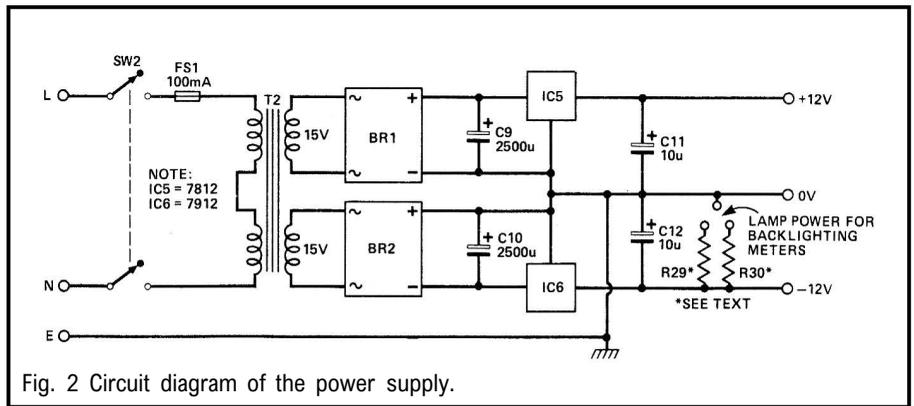


Fig. 2 Circuit diagram of the power supply.

through R and therefore to the current through the transformer. It seems perfect.

The killer here is the op-amp's offset voltage. In an attempt to maintain its inputs a few mV apart via the very small resistance of the coil, most of the amplifier's output current capability can easily be used up and a large voltage offset will be generated across R.

Offset trimming can reduce the problem to manageable proportions but the DC stability would get very little help from the feedback loop and so offset drift with time and temperature would make the circuit totally unreliable. Introducing a capacitor in series with the transformer is out of the question because of the phase shift and resonance peak that would be introduced.

The underlying characteristics of the circuit are so close to ideal

to an alternative solution.

Although an op-amp will have difficulty in cancelling an offset of a few mV, it might more easily cope with a few uV. Op-amps with input voltage offsets of the order of a few uV do exist but you'll need a second mortgage to be able to afford one. However, there are some reasonably priced amplifiers which include an internal auto-zeroing circuit.

Such amplifiers vary in detail from device to device but the essence of their operation is that the signal is processed by one amplifier whilst a second amplifier alternately cancels its own offset and the offset of the main amplifier, switching at a rate of 1kHz or so.

Unlike the circuit of Fig. 3, the offset is sensed at the input rather than the output and some fiendishly clever circuitry prevents the input signal from being

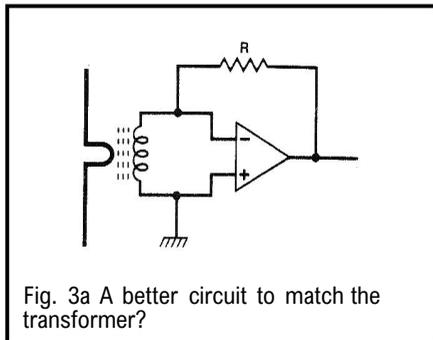


Fig. 3a A better circuit to match the transformer?

that it seemed to be well worth the effort of trying to get around the offset problem. The circuit of Fig. 3b gave quite encouraging results. In this the offset is cancelled by maintaining the mean level of the output at zero using a second op-amp. The compromise between settling time and low frequency phase shift was on the borderline of acceptability and it seems likely that replacing the integrator with a second order low pass filter would give a viable circuit. However, concern with phase, even below 20Hz or so, led

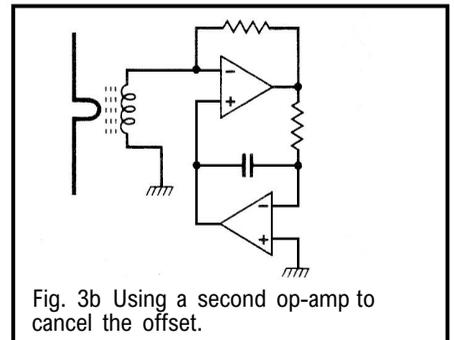


Fig. 3b Using a second op-amp to cancel the offset.

mistaken for an offset (at least it does in the Intersil ICL7650 but since the data book does not include the circuit of the IC, I can't be more specific about its operation).

A circuit based on the ICL7650 gave good results but was very sensitive to component values and lacked the solid and reliable 'feel' that a good circuit ought to have (or so John Bird tells me). On balance the circuit of Fig. 1 gave the best and most reliable results, and so was chosen for the final version.

## Go Forth and Multiply

To give a power reading, the voltage and current signals have to be multiplied together. There are several ways to achieve this. One possibility would be to use a pair of log-law amplifiers, sum the outputs, then apply the result to an anti-log circuit.

This would give single quadrant multiplication and with a bit of clever switching this could no doubt be extended to a full four quadrant multiplier. However, the thought of the half dozen or so critical adjustments is enough to make anyone shudder, let alone the complexity of the resulting circuit!

Most ETI readers will be aware that transconductance amplifier ICs will multiply after a fashion and they are commonly used for this purpose (see the power meter in ETI March 1984, for example). Better results can be achieved with the various special purpose multiplier ICs. The Intersil ICL8013, the Motorola MC1494/5 and 1594/5, the Analog Devices AD531/2/3/4 are some examples.

These devices are split into two main groups — most use techniques similar to the transconductance amplifiers, while a few are based on a translinear cell as shown in Fig. 4. If the transistors are perfectly matched, the relationship  $I_1 \times I_3 = I_2 \times I_4$  holds between the collector currents of the four transistors, giving the basis for both multiplication and division. The matching requirement means that it is not practical to build an accurate multiplier from discrete components (unless you are prepared to sort and test a bag of 1000 transistors!) but in an IC linearity of 1% or better can be achieved without difficulty.

The multiplier chosen for this project was a Silicon General SG1495, which is a transconductance type. With careful choice of components it has very good linearity. It is also readily available and not too expensive. The main rival was the ICL8013, which is easier to use and requires fewer external components (IC4a and its associated resistors in Fig. 1 would not be needed, for instance), but the superior high frequency performance of the SG1495 tipped the balance in its favour.

Figure 5 shows a simplified version of the internal circuit of the SG1495. This circuit is the basis of almost all transconductance multipliers and

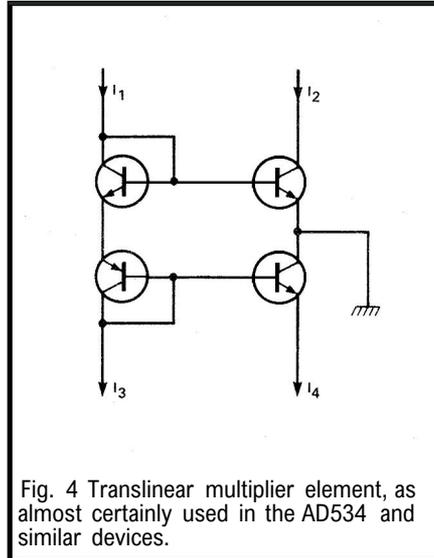


Fig. 4 Translinear multiplier element, as almost certainly used in the AD534 and similar devices.

provides an XxY output at pins 2 and 14.

## Construction

Winding the toroidal transformers is the most time consuming part of the construction, but it's worth taking some time over it. Cut off about 8ft of 0.1mm enamelled wire and tack one end to the core with a little superglue, leaving a tail of two or three inches for connecting to the PCB.

The first 99 turns out of the 100 total are the worst. You'll have to feed the entire length of wire through the toroid, being careful not to get kinks in it, and not to wear away the enamel by scraping it on the core. Patience!

Wind as evenly as possible around the core with no lumps of wire in one spot and bald patches

in another. Bring the coil to an end with another tail of two inches or so, about 5mm from the first. Hold it in place with another spot of Superglue.

Solder one end of the primary (0.4mm enamelled wire) to the PCB at point A. Thread it through the centre of the toroid and then through hole B, smoothing it down so that it forms a neat and fairly tight loop over the top of the secondary winding. Solder the ends to the PCB.

Thread the secondary connections through holes C and D and solder in place. The toroid should be held quite firmly in place by these connections. If not, another dab of Superglue will do the trick.

The preset pot positions on the PCB allow for either carbon skeleton presets or open cermet to be used in the outer holes, or enclosed cermet in the inner holes. I would recommend the enclosed cermet, but if the bank balance won't stretch that far, carbon types will do. (You can always 'upgrade' them later!).

The transformer is held in place on the PCB by its pins. For domestic use this should be all the support it needs, but if you intend to hump the meter around for use with PA or group gear, I would advise giving it extra anchoring with four N0.6 x 3/8" self-tapping screws, which fit into the corners of its case. You may also like to fix the smoothing capacitors firmly with some double sided adhesive pads.

Details of front panel arrangement are for you to choose. You can follow our layout

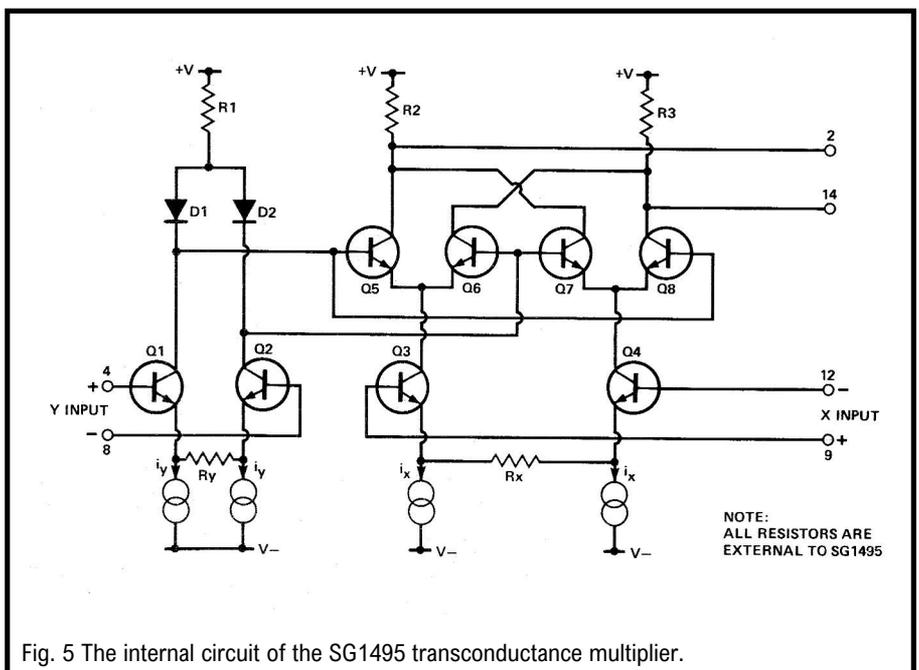


Fig. 5 The internal circuit of the SG1495 transconductance multiplier.

## PARTS LIST

RESISTORS (all 1/4W 5% carbon film unless specified)

R1,101	0R22 metal film
R2,102	470R metal film
R3,103	470R
R4,104	47k 1% metal film
R5,105	24k 1% metal film
R6,8,106,108	470k
R7,9,107,109	22k
R10,110	180k
R11-15,111-115	47k
R16,116	39k
R17,18,19,117,118,119	3k3
R20,21,25,120,121,125	10k
R22,23,26,120,123,126	2k2
R24,124	2k0
R27,127	8k2
R28,128	4k7
R29,30	Choose to suit backlighting

RV1,2,101,102	10k horiz. preset
RV3,103	500R horiz. preset
RV4,104	5k horiz. preset

CAPACITORS	
C1,3,101,103	10n ceramic
C2,102	4p7 ceramic
C4,5,104,105	470n 100V AC polycarbonate
C6,7,11,12,106,107	10u 16V tantalum
C8,108	470u 16V electrolytic
C9,10	2200u 25V electrolytic

### SEMICONDUCTORS

IC1,101	NE531
IC2,102	SG1495
IC3,103	TL074
IC4,10,4	NE5532
IC5	7812
IC6	7912
D1	1N4148
BR2,1	DIL bridge rectifier

### Miscellaneous

M1,101	1mA FSD meter movement
SW1/101	4 pole 2 way switch
T1,101	see text
T2	PCB mounting mains transformer 6VA 0-15,0-15

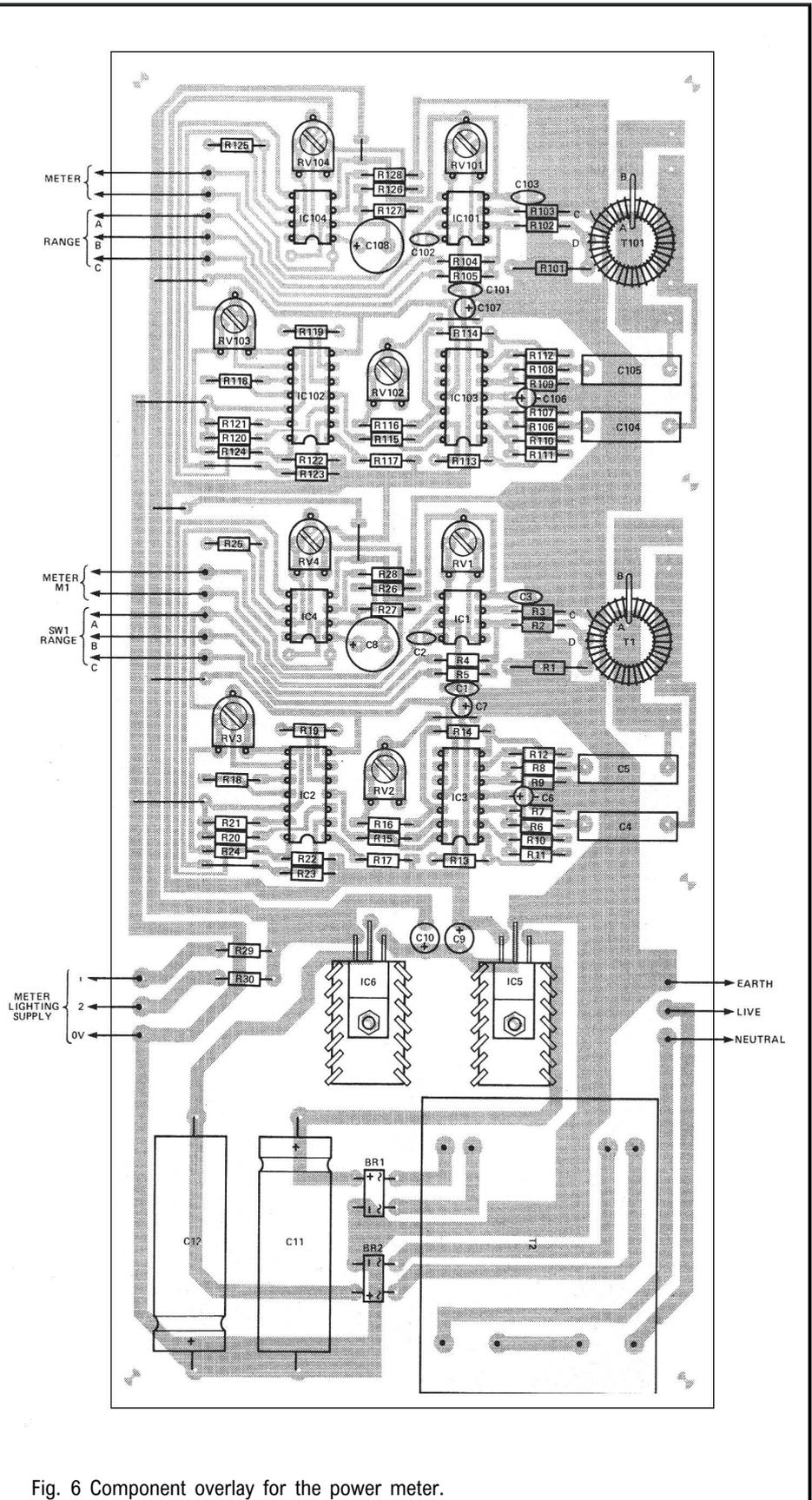


Fig. 6 Component overlay for the power meter.

from the photograph, or alter it to suit yourself. A suggested layout for the internal wiring is shown in Fig.7. If you don't follow it exactly, there are a few things to bear in mind.

Keep the mains wiring as far away as possible from the sensitive parts of the PCB (the toroids and IC1). Keep the range switch connections as short as possible. Don't forget to fit a fuse and a good earth connection to the case.

Use the best meters you can afford for the project — they are the main limiting factor in the

accuracy. The ones we used were from Electromail, and with all the accessories they cost about £30 each.

There is no need to follow our example. Any 1mA meter movement will do but to use a £5 'budget' movement would be

spoiling the ship for a ha'porth of tar.

If the meters you use have provision for back lighting, a supply for this purpose is available on the power supply section of the PCB. The resistor values you need will depend on

## BUYLINES

The parts for this project are almost all obtainable from Electromail. The transformer is stock No. 208-282. The case we used was a Centurion instrument case, type DX5, from Cirkit. The toroid is the only part likely to cause problems. Cirkit should be able to help here. The PCB is available from the EII PCB Service.

the choice of bulb, but I'm sure I don't have to tell ETI readers how to wire up a light!

## Setting up

Before turning on the meter set RV1 (RV101) and RV2 (RV102) to mid position, RV3 (RV103) to minimum resistance and RV4 (RV104) to maximum. Disconnect both meters and turn on the power. With your multimeter on the 10mA range, check that both meter outputs are giving less than 1mA. If it won't go low enough, turn off the power and check the circuit thoroughly.

Adjust RV3 to give a zero current reading. Set your multimeter to the 1mA range, connect up your amplifier and loudspeaker and check the reading rises as you turn up the volume.

Disconnect the loudspeaker but leave your amplifier connected. Set your multimeter to a sensitive current range (100µA or less). Set RV3 to give a reading roughly in the centre of the meter scale. Turn up the volume control on your amplifier watch for any movement in the meter needle. RV1 must be set so that with no speaker connected, the output remains constant regardless of the volume setting on your amplifier.

With RV1 at one end of the scale the meter will move in one direction as the volume increases. At the other end of the scale the meter will move in the opposite direction. Somewhere in the middle, it won't move at all.

Each time you try a new setting for RV1, adjust RV3 to bring the meter needle back to centre scale and turn the amplifier volume up and down. When you find the position where the meter needle does not move, you've found the correct setting for RV1.

Having set RV1, adjust RV3 to give a meter reading of zero with your amplifier disconnected. Connect up the power meter's own meter movements. Connect a 10 ohm resistor across the output of the power meter. I would

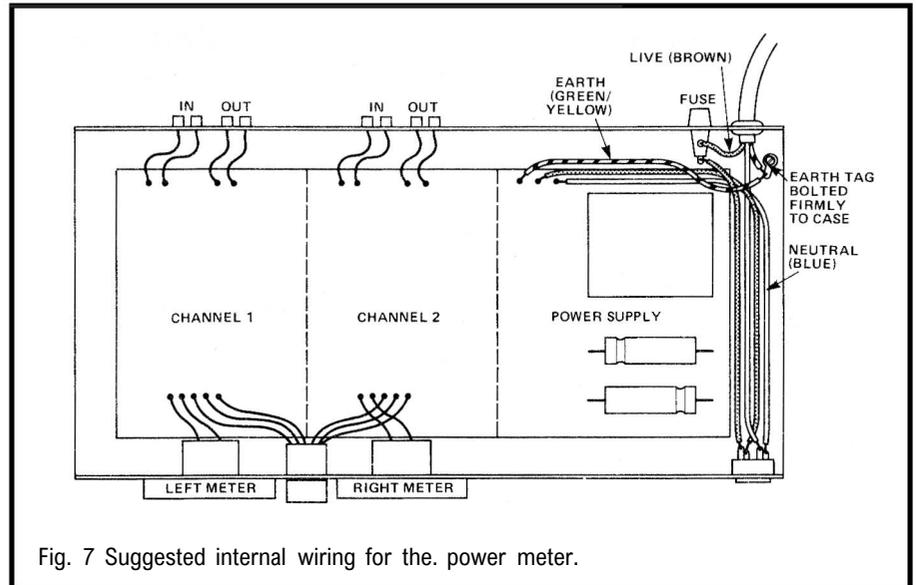


Fig. 7 Suggested internal wiring for the power meter.

suggest using the 17 watt ceramic resistors available from Electromail — a pack of 5 costs around £1.50. Use a series/parallel arrangement of four 10R resistors to give a 10R resistor which can handle 68W.

Connect a sine wave oscillator or signal generator to the 'Aux' input of your amplifier. A suitable sine wave oscillator was given in last month's article. Connect your multimeter across the resistor on at least a 20V AC voltage range and turn up the amplifier's volume control until it reads 20V. At this point you can set the meter to read 40W on the 50W range by adjusting RV4.

If you are lucky enough to have a meter with an accurate AC current range, you can connect it in series with the 10 ohm resistor and, with the amplifier volume control in the same position, make a current reading (Don't burn your fingers on the resistors!). Multiplying the current you get by the 20V you set will give you a power reading independent of the accuracy of the resistor value. Set the power meter to the result of your calculation via RV4.

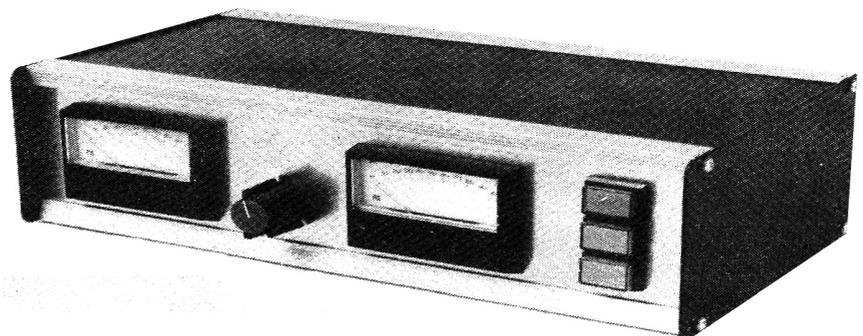
Only one calibration is necessary. The meter should now read correctly on both power settings.

If you are keen to check, you can make readings at other power levels and make sure that the power meter agrees. Either multiply the RMS voltage and current readings together, or square the voltage reading and divide by ten (for a ten ohm resistor).

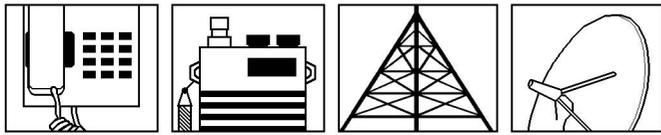
You'll notice I haven't said anything about setting RV2. This makes very little difference to the readings, and should be left at the centre of its travel. If you are a perfectionist and have a signal generator and oscilloscope, you can set it up (before making any of the other settings) like this.

Short together the speaker connections on one channel, then connect your signal generator between these connections and the PCB ground. Connect your oscilloscope to display the output from pin 14 of IC3 and adjust RV2 for the minimum output. Then do the same for the other channel.

If you would like to check that the meter does indeed reject the reactive component of the power, you can try running it with a capacitor across the output. A quick search around with your 'scope will show that voltage and current signals are present in the power meter circuit, but the meters move not a jot.



# OPEN CHANNEL



Long ago the term was VANS (value added networks). These were communications-based networks connected to the existing public telephone network which could be accessed by individuals or organisations and which added value to the network. In other words, any network which a user can dial into through the PSTN — videoconferencing, teletex (*not teletext* that is), certain viewdata networks and electronic mail services, and so on.

Because the term didn't appear to be including data networks and maybe for a few other reasons, too, the Department of Trade and Industry have started to call such networks VADs — valued added and data services. The DTI policy since renaming these networks has also been to broaden the categories of services which are included under the banner, such that any bureau holding a database of any description which can be remotely accessed over the PSTN is now classed as a VAD.

Under the old VAN title, it was often taken that the network must be accessible with the user's own data equipment. But the VAD title no longer assumes this. In fact, even good old TIM, the speaking clock (a database by any other name?) is now a VAD.

A special programme, recently launched by the DTI to promote VADs is a good source of information for prospective users. Contact: DTI, Information Technology Division, 29 Bressenden Place, London SW1E 5DT.

## The Number Game

At one stage, it was thought that users dialling into or out of Mercury Communications telephone network, which is rapidly being constructed to compete with BT's PSTN, would have to dial a prefixed number before the actual telephone terminal number.

If a Mercury user in London wanted to call a BT user also in London, the Mercury user would have to dial the London prefix (01), then the BT user's normal seven digit number. This has all changed.

Mercury has always fought against a prefix, on the grounds that a user's telephone number is the property of the user - not the service provider.

The fight has now paid off. A recent agreement between BT and Mercury gives Mercury users numbers of the same form as BT

users. The other telephone network service providers, on the other hand (Vodafone and Cellnet) have no such agreement and their users are still lumbered with required prefixes (or is it preffices?).

## All In the Exchange

Many moons ago, I reported on a new type of telephone exchange connection which could effectively decimate small to medium users' telecommunication bills. It was to be called Centrex.

Generally, exchange connections at present are through private automatic branch exchanges (PABXs). With a PABX, a company has an internal telephone network, with a number of extension terminals but only a restricted number of exchange lines. The number of extensions and the number of exchange lines depends directly on the PABX used. To dial another extension, a user simply dials the extension user. Dialling out onto the PSTN, however, is a matter of dialling a prefix number (typically, 9) to get 'an outside line', then dialling the required telephone number. Users can either buy or rent the PABX equipment.

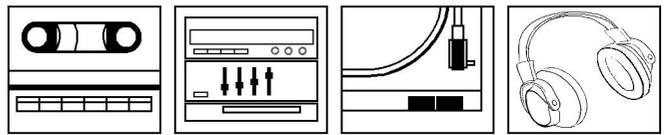
With Centrex, on the other hand, no PABX equipment is required. Instead, part of the local exchange becomes allocated to the user as a quasi-PABX. This means that all 'internal' calls as well as those dialled out are actually made through the local exchange. This, in turn, means that a greater number of exchange lines are required, but generally costs will be down.

Centrex also has the advantage of flexibility. Some services which cannot be included through a PABX (or which can only be included if the PABX is highly specialised) can easily be incorporated via Centrex. Furthermore, the addition of extra extensions or facilities (say, if the user's company is growing) can be incorporated without delay or the need to exchange obsolete equipment.

Although commonplace in (guess where!) North America, it's taken a bit of time to reach the UK. However, it's looks as though Centrex is on its way here at last. Users should be on the look out for Centrex services (probably launched in the City of London) by the start of next year.

Keith Brindley

# PLAYBACK



The imminent arrival of DAT (digital audio tape) on the consumer market has record companies worried. They believe that DAT will encourage home copying on such a scale that record, cassette and CD sales will slump. There are reports of an effective 'spoiler' system, which protects copyright recordings with a signal in the audio band.

Such a signal could not be (illegally) filtered without damaging the audio quality but it is claimed not to affect the sound otherwise. An audio signal which can neither be heard nor filtered seems a remarkable thing.

## This and DAT

DAT is a system for recording sound to 16-bit accuracy on a small format tape cassette, using a rotating, helically scanning head. Playing time could exceed two hours, as against 70 minutes on a Compact Disc. However, players are likely to cost around £800 and may not be available for one or two years yet.

The market penetration of CD is so far only around 5%. A representative of the British Phonographic Institute (BPI) tells me this is because most people will happily listen to poor quality sound — a factor which also allows bootleggers and home recording to flourish. But, she said later, DAT, with its CD-like quality, will encourage a boom in home taping.

Home taping, says the BPI, is far more of a problem than bootlegging (unlicensed copying of recordings for resale). The record industry believes that six times more music is copied in the home that is actually bought. 81 million blank cassettes were imported last year. Many of these are used for computing and for copying speech and non-copyright music but the record industry knows that people are taping records at home because they admit it. It would like them to stop.

The industry has an important point in its favour. Its expenses are vast. An enormous amount of money is needed to sponsor, develop, record, promote and market the artistes who bring in the capital. If the customers steal the product without paying for it, one day there will be no industry and no product. Everybody loses.

The record industry has pressed for a levy on blank tape

to cover lost royalties. This has not happened yet but legislation is under consideration in the UK, the USA and in the European Parliament.

DAT worries them even more than this. They want to forbid the manufacture or import of DAT recorders unless these incorporate a circuit inside the main LSI chip which will search for a special signal in new copyright material, and switch off the recording.

DAT manufacturers say that they will use a different sampling rate from CD, so that direct digital recording will not be possible. The signal will have to be converted to analogue and back. In this case, any spoiler using signals outside the audio range can be thwarted by filtering out the signals.

The spoiler system invented by CBS works by cutting a notch out of the audio spectrum at a frequency above the top fundamental of most instruments. The notch is switched in and out in a pattern that the recorder recognises.

Already, there is a bizarre rumour that non-protected recordings will be made available, at a much higher price.

The record companies are also worried that even if DAT is 'spoiled' it will split the market away from their investment in CD. This is not a problem for the Japanese because CD has already peaked there. Their manufacturers need DAT as the next boom item.

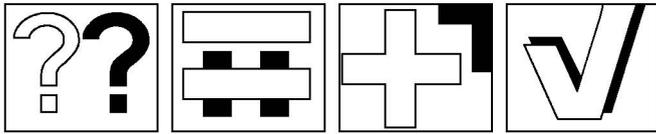
## Myopia

Trying to raise market share by restricting access to new media strikes me as a short sighted view. I doubt that there is a one-to-one relationship between records casually copied and lost sales. Buyers have only so much money to spend and most would rather choose a properly packaged piece of vinyl for essential musical purchases, only making-do for non-essentials. If the going gets tight, they are likely to decide that they can do without.

The record companies have principle on their side but there does seem to be a place for allowing customers to copy their purchases for private use, if only to maintain a degree of goodwill towards the music business in general. If a consumer industry wages war on the consumer both sides are likely to lose. DAT will lead to MAD.

Andrew Armstrong

# ALF'S PUZZLE



The news that Alf was leaving came as a shock to all of us. Things just won't be the same around the ETI offices without his coffee stains on our circuit diagrams and his half baked ideas to keep us all amused. 'Never mind, Alf; we told him. 'One day next week we'll have a surprise party for you.'

That very afternoon, John Bird came across Alf looking utterly miserable. 'Cheer up, old chap,' said John. 'You can always change your mind, you know.'

'It's not the thought of leaving that's upset me,' moaned Alf. 'It's just that I've worked out that there won't be a party for me.'

'What makes you think that?' asked John. We've told you we're going to arrange one for next week but we can't tell you the day or it won't be a surprise.'

'That's just it,' said Alf. 'If it's got to be a surprise, I can't have a party at all. If you arrange it for Friday it won't be a surprise because on Thursday I'll know that it *must* be tomorrow. But if you arrange it for Thursday, it won't be a surprise because on Wednesday I'll know that it can't be on Friday, and so I'll be expecting it on Thursday. But since it won't be a surprise if it happens on Thursday or Friday, on Tuesday I'll know it's got to be on Wednesday, so that won't be a surprise either. The same applies to Tuesday, so I'm expecting the party on Monday. But then if it is on Monday that won't be a surprise either, so I can't have a surprise party at all.'

'I dare say you're right,' said John.

Alf's party was on Thursday, and since he wasn't expecting one at all, he was surprised!

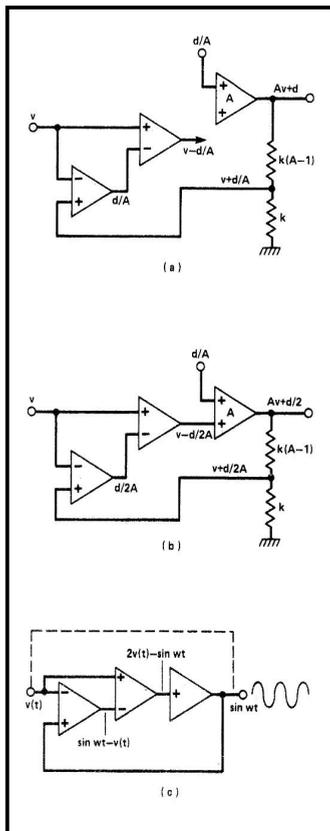
## April's Puzzle

If you followed the reasoning behind the April issue puzzle, I'm sure you have had not the slightest difficulty in spotting the fallacy. If you complete the loop in Fig. 1a (reproduced from last month), the distortion is actually halved, not reduced to zero (Fig. 1b). It seems that we are still getting something for nothing — half the distortion without loss of gain. Is this an improvement on negative feedback or just another illusion? (The reduction in distortion is real enough, but is the apparent advantage over NFB genuine?) I'll leave you to work out that one for yourselves.

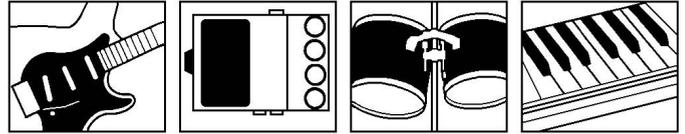
In case you think the bizarre conclusions are a result of Alf's 'muddling', here's a little sleight of hand without the controversial imaginary input. First of all, take Alf's circuit and decide what you'd like the output to be. Let's say a sine wave. We don't know what the input is at the moment, so we'll just call it  $v(t)$ . Fig. 1c shows that Alf's circuit will feed an input of  $2v(t) - \sin(\omega t)$  to the input of the amplifier (I've made it unity gain and got rid of the resistors for clarity — you can put them in if you like).

If we feed the output back to the input we now know what  $v(t)$  is: it's  $\sin(\omega t)$ . The input to the amplifier is now  $2\sin(\omega t) - \sin(\omega t) = \sin(\omega t)$ , giving an output of  $\sin(\omega t)$  which is fed back to give an input of  $\sin(\omega t)$ , which produces an output of  $\sin(\omega t)$ ...

OK, so there's nothing special about a sine wave generator, but I chose the sine wave completely at random. A lucky choice? Try it with a square wave, or anything else you choose — it will sustain any waveform whatsoever! The ETI universal function generator will *not* appear as a project, for reasons I'll leave you to work out for yourselves.



# KEYNOTES



Frederick the Great, King of Prussia, was a busy man well known for his success in military defence strategy and international politics. Despite these obviously taxing commitments he was also a highly competent and active musician with a keen interest in any new music technology.

When a brand new synth known as the Piano-Forte came on the market, King Fred bought one immediately and was so enthralled by its sound synthesis capabilities that over the following years he purchased no less than 14 more in order to stay abreast of endless design updates.

Pianos soon became all the rage in Europe. Even J.S. Bach dropped in at the palace one evening to try them out. The rest, as they say, is history.

The piano has either two or three oscillators per note, a velocity-sensitive keyboard and a single (preset) output filter. Timbre is essentially fixed, envelope control limited, recalibration is required frequently, transportation is impractical and MIDI retrofits are unavailable.

It is therefore rather interesting to note that the machine is still widely acclaimed to be the best keyboard around and remains in production today, even in Japan.

It has to be said that there is more to the popularity of the piano than mere conservatism or nostalgia — beyond any shadow of a doubt its sound has a subtle and elusive quality that seems to defeat the best electronic instruments altogether.

## Unnatural Practices

It is often argued that electronic instruments are unnatural. All musical instruments are contrived artifacts which at their time of development represented high technology.

It is normal for any new type of instrument to have its own characteristic sound and certainly this has always been true of synths. A synth sound is almost invariably recognisable as such and certainly not displeasing when used with creative imagination in an appropriate musical context.

The saxophone, electric guitar and synth have all been initially blamed of sounding unnatural, before being granted a grudging acceptance into the world of purists and stuck-in-the-muds. But

the story does not quite finish there.

Over the course of time public familiarity with electronic music has led to the use of the word electronic as an appropriate adjective to describe any sound that is monotonous and lifeless or machine-like. This sentiment is very widespread and cannot be attributed entirely to unimaginative use of the instrument as has often been argued.

## Good Character

Descriptions like *soul*, *character* and *expression* do no more than hint vaguely at the exact technical nature of the problem, even though their subjective meaning is intuitively quite clear. The best that we can do at the current time is to treat the output signal with chorus and reverb effects in order to obscure its intrinsic deficiencies.

This state of affairs is indeed a poor show for a machine that originally held forward the promise of being able to synthesise any given sound.

Synthesis techniques are frequently pigeon-holed into three categories — subtractive, additive and contrived. Contrived techniques are pragmatically defined as those which do not fit in either of the other two groups and include methods such as FM, waveshaping and discrete summation formulae. However, there are not yet any popular techniques in any of the three categories which are capable of accurately modelling acoustic instruments in practice.

A possible exception is additive synthesis — the sledge hammer method of painstakingly building up a sound out of individual sine waves, each with its own intricate frequency and amplitude time envelopes. However, many acoustic instruments can only be satisfactorily imitated by specifying upwards of a hundred of such components, rendering additive synthesis as laborious to the musician as it is demanding of the hardware.

So what synthesis technique do acoustic instruments themselves use? Partial differential equations which 'acousticians' have not yet done enough work on.

Far from coming to maturity, music synthesis is merely leaving its infancy

Bruno Hewitt

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	Board	H
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	Board	R
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E8604-2	Matchbox Amplifier	C
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	Version	C
E8604-4	MTE Analogue/Digital	M
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E8605-1	Microlight Intercom	E
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E8605-4	Portable PA	H
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E8606-2	Midi-CV Converter PSU	D
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E8706-1	Hi-fi Power Meter	N
E8706-2	MIDI Keyboard CPU	U
E8706-3	MIDI Keyboard Front Panel	O
E8706-4	Flame Simulator	G

### Digital Audio Selector (November/December 1986 and January 1987)

In Fig. 5 (December 1986) the resistors shown as R14 and R114 should be R19 and R119. This error is continued in the discussion of gain setting in the January 1987 issue.

The DG507A IC used in the prototype came from Farnell Electronic Components of Leeds, Tel: (0532) 636 311 Farnell normally deals only with trade customers but private orders are sometimes handled at the company's discretion. Trilogic of 29 Holm Lane, Bradford BD4 0QA, Tel: (0274) 684 289 will obtain any Farnell component to order on payment of a 25% handling charge. The Farnell order code is simply the full device number DG507ACJ.

### Biofeedback Monitor (December 1986)

The capacitor C4 is shown the wrong way around in the component overlay diagram (Fig. 4).

### The Intelligent Call Meter (December 1986)

The hex dump listing of the ROM for this project (Table 3) was badly printed. The byte at location BF should read ?F.

### The Better Flanger January 1 1987)

In the circuit diagram (Fig. 2) D1 is not labeled. This is connected to Q1. In the component overlay (Fig. 5) several components are missing. A link should connect the two pads to the left of C1. Q1 is situated next to D1 and connection point P4 is situated between R16 and R33. In addition, the positions of R16 and C11 should be swapped.

### Photo Process Controller (February 1987)

In the circuit diagram (Fig. 2) the cathodes of diodes D3,5 are shown connected to OV. They should connect to the junction of R16,17,18. In the overlay diagrams (Figs. 3 and 5) the flying leads are numbered incorrectly. Leads 7, 8, 9 and 10 at the top of Fig. 3 should be numbered 16-19. In Fig. 5 leads 6 and 8 from the top of R13 should be numbered 16 and 17. Numbers 9 and 10 from Q1 and Q2 should be 18 and 19. In addition the leads 11 and 'A' should be swapped.

### Capacitometer (March 1987)

The circuit diagram (Fig. 1) should show pin 1 of IC1 connected to OV. The zener diode (ZD1) should be connected between the junction of R10/R11 and OV. The PCB foil is correct.

### BBC Micro MIDI Interface (April 1987)

IC7 and IC8 (the 6N139 opto-isolator ICs) are missing from the parts list. In the Buylines section it is incorrectly said that these are available from Electromail as part 302-126. The isolator is available from Maplin as part number RA59P. Resistors R8,9 are missing from the overlay diagram (Fig. 4). These are located in the two pairs of pads below IC6. There should also be no OV connection to the MIDI IN sockets, only to the OUT sockets (pin 2 so as to prevent earth loops).

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BC182	12
BC182B	12
BC183	12
BC183B	12
BC184	12
BC212	12
BC212B	12
BC213	12
BC213B	12
BC214	12
BC327	16
BC337	16
BC548	12
BCY70	22
BCY71	22
BD131	60
BD132	60
BD135	34
BD136	35
BF258	60
BFX85	40
BFX88	40
BFY50	37
BFY51	37
BFY52	39
TIP31	42
TIP31A	48
TIP31B	56
TIP31C	54
TIP32A	42
TIP32C	42
TIP33A	100
TIP41A	63
TIP42A	55
TIP3055	76
TIP2955	76
ZTX300	17
ZTX500	17
2N3053	60
2N3054	160
2N3707	12
2N3703	12
2N3705	12
2N3771	140
2N3904	15
2N3906	15

## DIODES

IN4001	5
IN4002	5
IN4003	6
IN4004	6
IN4008	6

## TRIACS

3 Amp 400V	75
8 Amp 400V	90

## OPTO ISOLATORS

TILTIL111 transistor o/p	110
TIL 113 Darlington o/p	120
3021 Triac driver	150

## LEDs

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Yellow	18
Green	18
Super bright t1¼ 5mm Red	35

## ZENER DIODES

BZY88C 500m W 4V7	10
10V	10
12V	10
BZX55C 500m W 24V	10
BZX85C 1.3 Watt 4V7	20
10V	20
12V	20
24V	20

## VOLTAGE REGULATORS

LM317T +1.2V to 37V	150
LM341P +5V	60
LM7905 -5V	70

## BRIDGE RECTIFIERS

W004 1.5A	50
6005 6A	90

## CAPACITORS

### Electrolytic

47uF 25V	10
100uF 25V	12
470uF 25V	28
1000uF 25V	36

### Tantalum

.1uF 35V	10
.22uF 35V	10
.47uF 35V	10
1uF 35V	10
2.2uF 35V	15
4.7uF 35V	20

### Ceramic

220pF 500V	6
470pF 500V	6
1000pF 100V	6
2200pF 100V	6
4700pF 100V	6

## RESISTORS

### Metal Film 5% 1/3 Watt

100R 680R 1K 1K2 2K2 4K7
5K6 6K8 10K 12K 15K 22K 27K
33K 39K 47K 56K 68K 82K
100K 120K 150K 180K 220K
270K 330K 390K 470K 560K
680K 820K 1M

2p

## SKELETON PRESETS

Horizontal	19
Vertical	19

## LINEAR ICs

741	18	NE5532	120	LM308	70
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556	65	ZN414	90		
LM301	28	ZN416	160		

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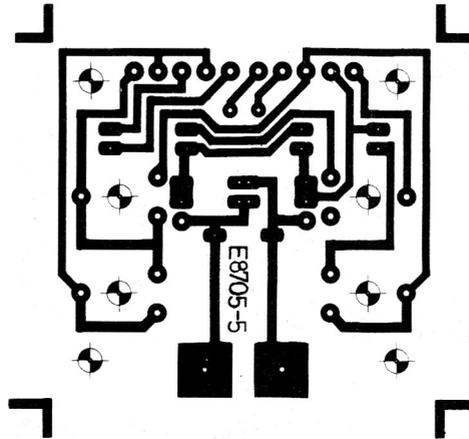
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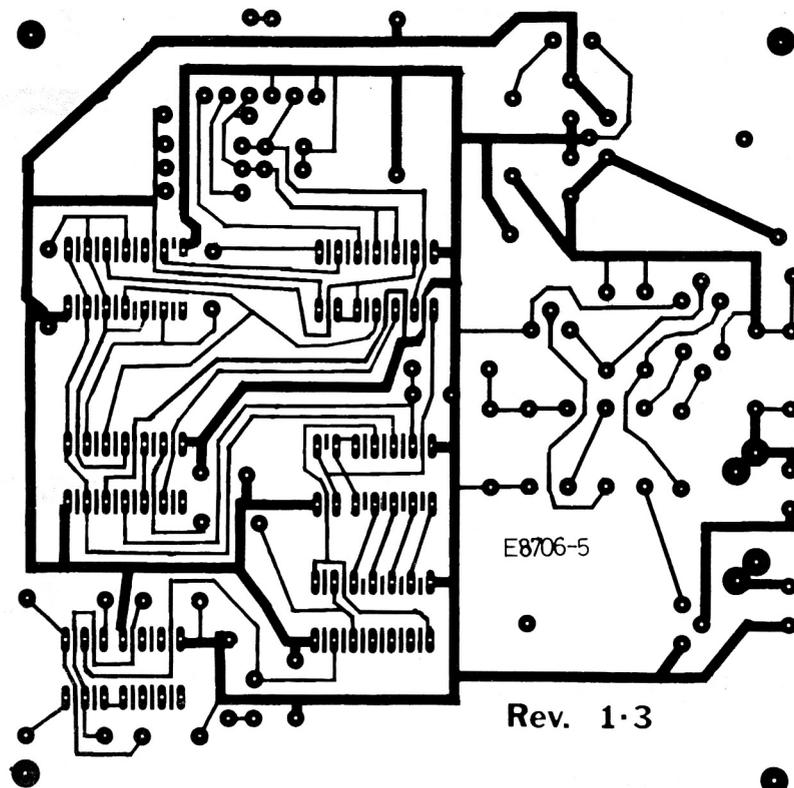
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# PCB FOIL PATTERNS

Due to lack of space the foil for the front panel board from the MIDI Master Keyboard has been held over until next month.

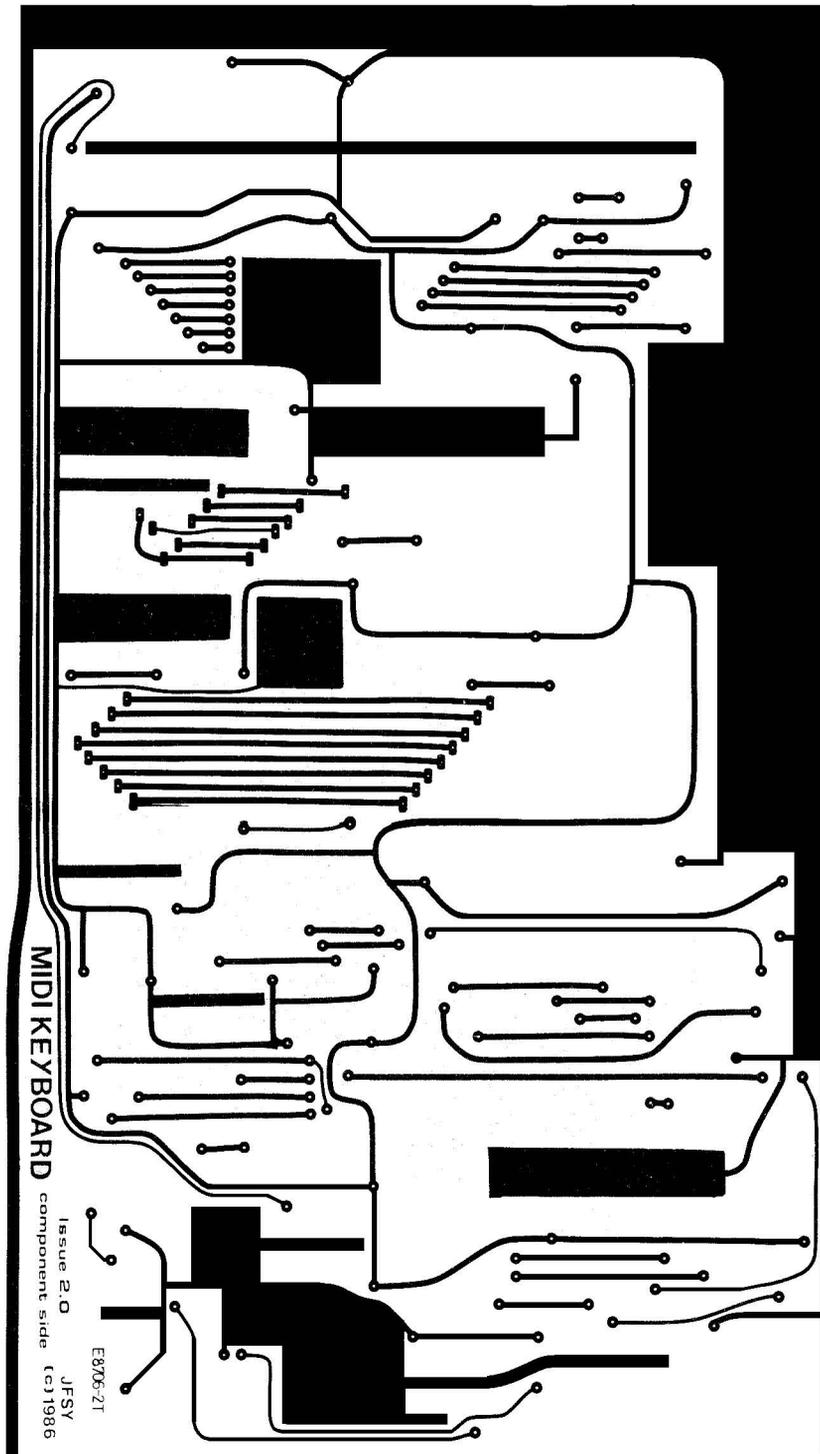


The foil for the budget power meter which was incorrectly given half full size last month.



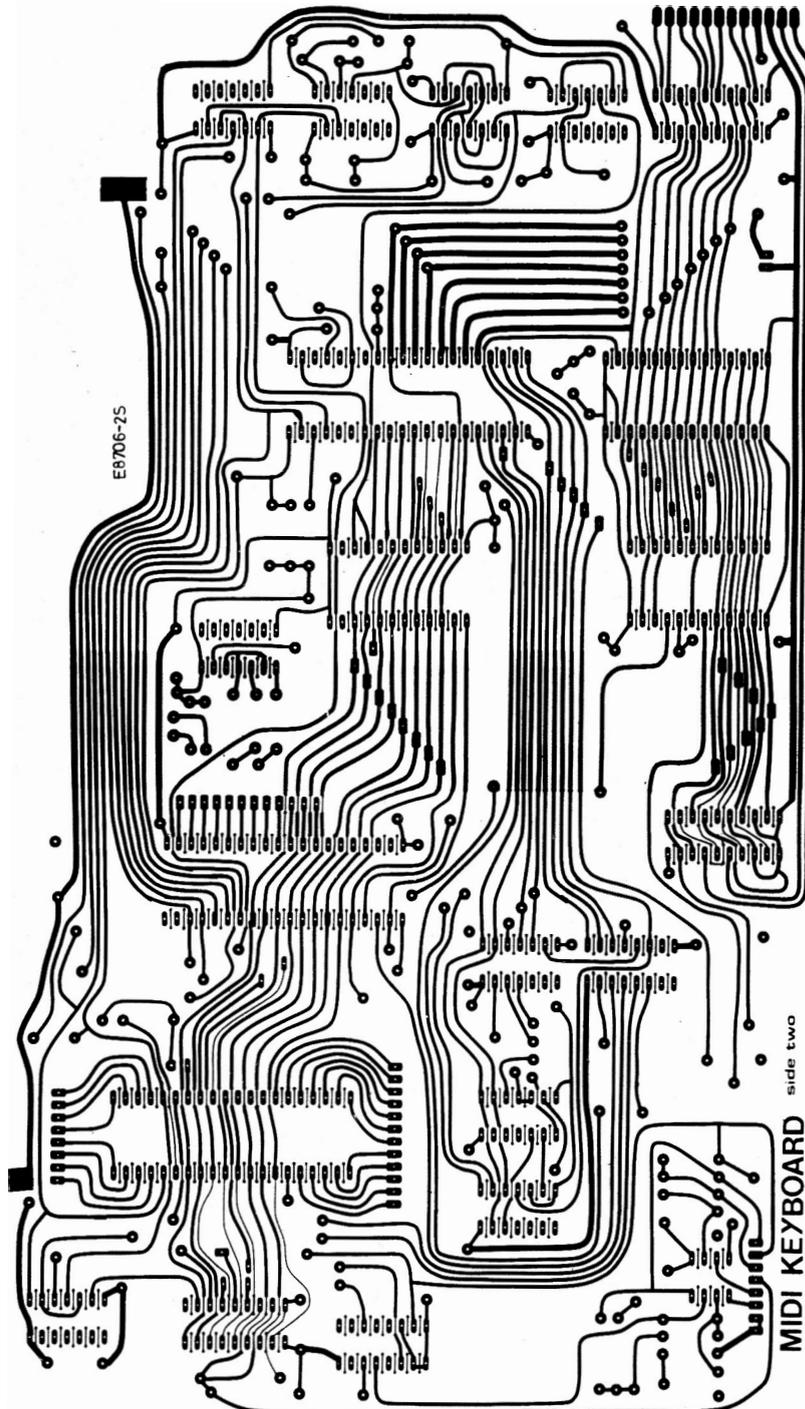
The Flat Alarm foil pattern.

# PCB FOIL PATTERNS



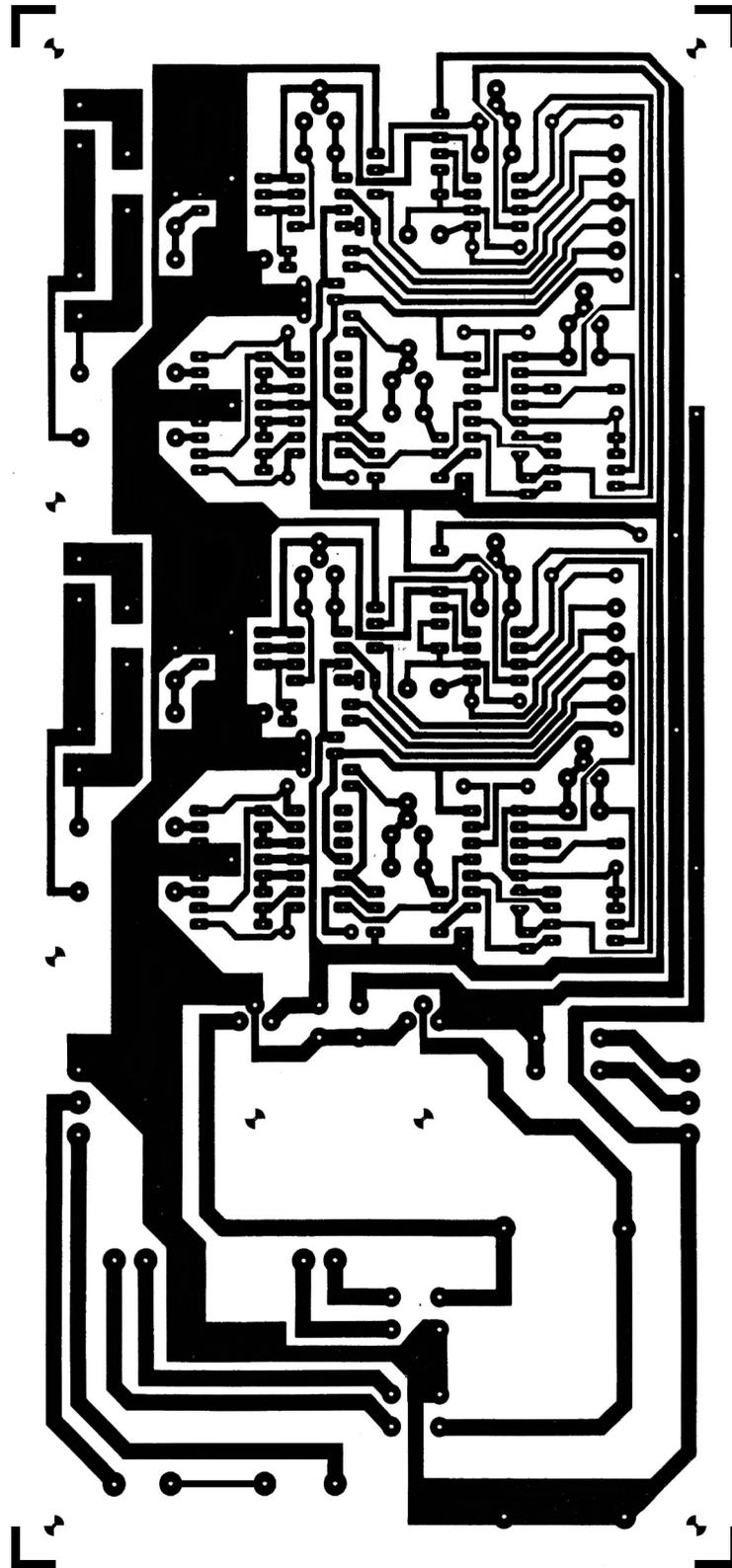
The topside foil for the MIDI Master Keyboard CPU board.

# PCB FOIL PATTERNS



The solder side foil for the MIDI Master Keyboard CPU board.

# PCB FOIL PATTERNS



The Hi-Fi power meter foil.

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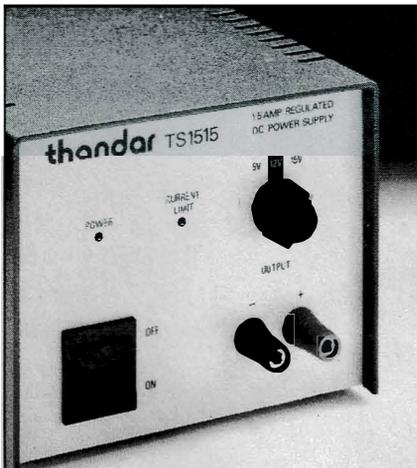
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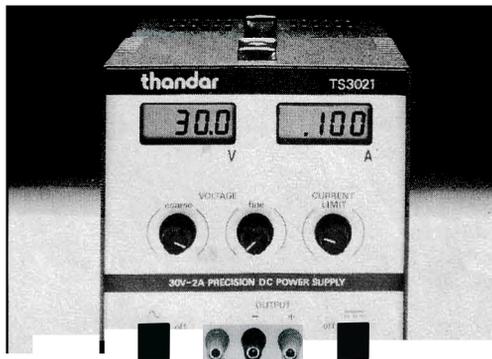
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TS1515

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Output switchable to 5V, 12V or 15V. 1.5A max; protected output. Line and load regulation <0.5%.



TS3021

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0-30V by coarse and fine controls. 0-2A by log control. Dual 3.5 digit LCD readout of V and I. Constant V or constant I Modes; protected output. Line and load regulation <0.01%. Ripple and noise <1mV; low radiated and conducted interference.



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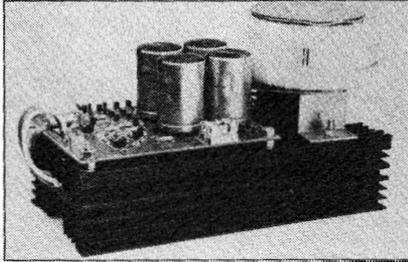
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#### 240W HIFI AUDIO POWER AMPLIFIER KIT NR. K2587

The introduction of MOSFET transistors in power amplifiers opened a new area in this field. Wide power bandwidth, low driving power, high output power and an almost ideal transient response are only a few of the advantages. This kit is based on this technology. Apart from the power-amplifier, it also includes the power supply, heatsink and transformer. Once assembled, its ready for use and can easily be housed. Only 2 final adjustments are required and only needs a multimeter.

- Some applications: Discobars and discotheques - Orchestra or theatre - DC coupled power controls.
- Power supply (including transformer) 2x45 VDC/5A
  - 240w music power at 4 Ohm.
  - Distortion (1kHz): 0.0%
  - Intermodulation distortion: 0.0%
  - Input impedance: 33K.

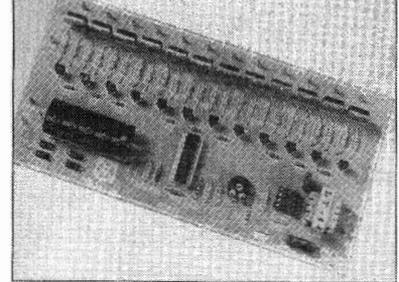
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## AUDIO LABORATORY DIY TEST GEAR COMPUTERS TOP QUALITY KITS FOR HOME CONSTRUCTION



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#### GIANT VU METER KIT NR. K2620

Several circuits providing different light effects, from the simple lightorgan to real 'lightcomputers', have already appeared on the market.

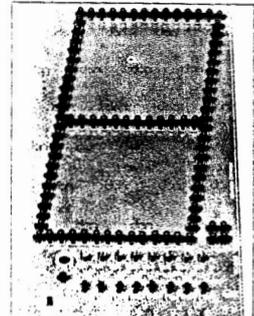
This kit is something new... a giant VU meter with 240V bulbs. The 12 bulbs are mounted as a lightcolumn which varies according to the sound level.

The input is galvanically separated and the sensitivity is adjustable, so there is no danger when connected to a pre-amplifier or to a power amplifier.

- 12 triac outputs: 400W each (non-cooled).
- Input impedance: ca. 20 Kohm.
- Input sensitivity: adjustable from ca. 100mV to 3V at full scale.
- Power supply: 9 VAC/0.5A.

Price £36.85 + p&p

### LIGHT UP THE SKY



#### 20CM DISPLAY 'COMMON ANODE' KIT NR. K2567

This kit contains a 7-segment display consisting of 12 leds per segment and 4 leds for the decimal point. With the aid of a supplementary power supply, it is possible to connect this kit to any existing circuit equipped with common anode displays of any brand and any dimension.

If the digit and segment drivers of the circuit can supply sufficient current, it will be possible to connect in parallel two or more displays, or even, leave the small display of the circuit in place and connect the 20cm display in parallel. This latter will not effect the brightness of the 20cm display due to the specila concept of the driver circuit.

- Common anode.
- Power supply: 22 to 26VDC non-stabilized.
- Minimum anode input voltage (on): 2V.
- Maximum anode input voltage (off): 1.2V.
- Segments input impedance: 10K.
- Segment current: static (R6=00): +40mA multiplex (R6=220hm): +75mA.
- Total current consumption in static mode: maximum 400mA.
- Maximum power (U=22V): 8.8Watt.

Price £30.26 + p&p

#### 20CM DISPLAY 'COMMON CATHODE' KIT NR. K2568

This kit is in terms of appearance and application identical to K2567 'COMMON ANODE'. As far as specifications are concerned; read cathode for anode.

Price £31.93 + p&p

K610	VU-LED MONO (UAA 180) USING LED'S	13.74
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K2580	POWER SWITCH&DIMMER (600 WATT UNCOOLED)	13.69
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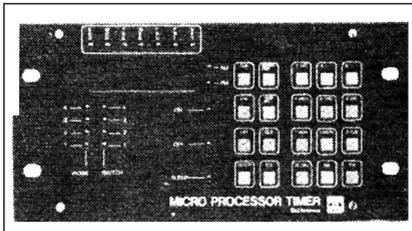
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## MICROPROCESSOR UNIVERSAL TIMER KIT NR. K1682

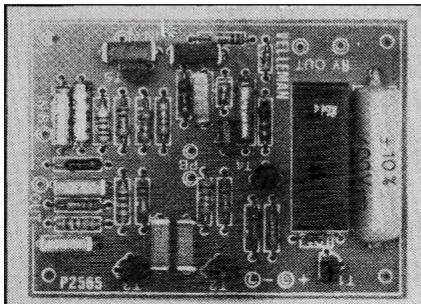


This unique timer is in principle a 24-hour clock provided with 4 relay-switched outputs and a programming period of 1 week. 20 switching programs can be memorized and via the membrane keyboard be programmed. Outputs or timing periods can be selected at random. All program steps are indicated by LEDs. A printed alu frontplate is included in the kit, making building-in of this timer a simple affair. This microprocessor timer was primarily designed for industrial and labo purposes, but the amateur can use it in dozens of applications as well.

- 20 daily- or weekly programmable timerfunctions.
- Memory display of programmed timer functions per output or per day.
- 4 independent relay outputs (1 relay included).
- Display of: day of week - AM/PM - output - clock.
- ON/OFF - sleep.
- The timer is based on the TMS 1122 microprocessor.
- Transformer 12VAC/1A (not included).

Price £75.85 + p&p

## TAPE/SLIDE SYNCHRONIZER KIT NR. K2565

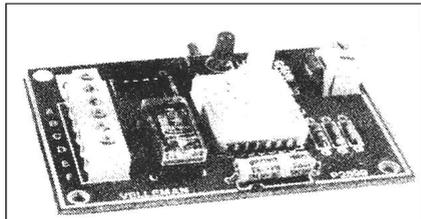


Actually, a lot of tape/slide synchronizers are available on the market. The price of these devices varies from expensive to very expensive. Those owning a tape- or cassette recorder can with this simple and inexpensive device, record synchronizing pulses and use these pulses to control automatic slide projectors. The circuit is small in size and can easily be housed.

- Power supply: 9 to 13VDC.
- Current consumption: 40mA.
- Output frequency (tone): +1.5KHz.
- Output amplitude: +250mV.
- Input sensitivity A: minimum 1.5V peak to peak.
- Input sensitivity B: minimum 100mV.
- Oscillator: AMV type.
- Input impedance (B): 1 KOhm.
- Output impedance: 15 KOhm.

Price £12.75 + p&p

## SCREEN WIPER ROBOT KIT NR. 2599



Three different time intervals may be selected by using a multipole rotary switch. With small component changes, the intervals may be varied. Some applications: windscreen wiper delay, diaproyector control, hazard warning via the braking lights of the car. In the manual you will find a complete description how to build this kit in a car, with wiring instructions to connect it to the existing wiper installation.

- Power supply: 12-15V DC.
- Intervals: 5-10-15-seconds.
- Relay output: 240V/2x3A.
- Relay output with two change-over contacts.
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- Output 'ON': 100mA.
- Dimensions: 82x56x41mm.

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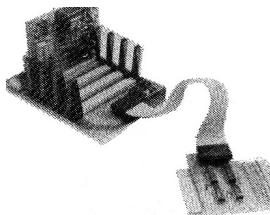
Even the smallest computer can afford powerful applications you wouldn't dare to imagine. Today we have 10 function cards in our system but tomorrow there might be more. And while using this system you keep all communication means originally provided on your computer.

### VELLEMAN INTERFACE SYSTEM - KITS

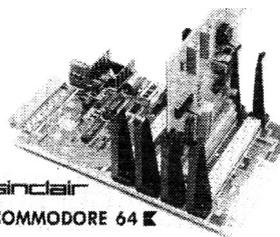
K2609 OC OUTPUT BOARD INTERFACE FOR HOME COMPUTER	22.60	K2631 EXTENSION BOARD FOR K2640 OR K264121.22	
K2610 A/D CONVERTER INTERFACE FOR HOME COMPUTER	35.55	K2633 RELAY CARD	15.25
K2611 OPTO INPUT BOARD INTERFACE FOR HOME COMPUTER	26.30	K2634 QUAD TRIAC SWITCH CARD	16.33
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K2629 REAL TIME CLOCK INTERFACE FOR HOME COMPUTER	41.35	K2612 RS232 MOTHERBOARD (I.B.M. COMPATIBLE)	123.34

### VELLEMAN INTERFACE SYSTEM - BUILT AND TESTED

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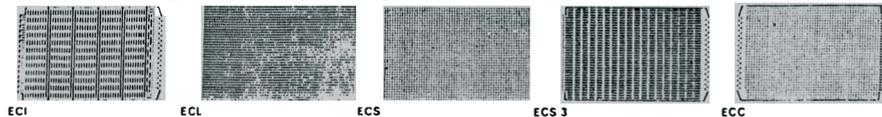


Sinclair  
COMMODORE 64

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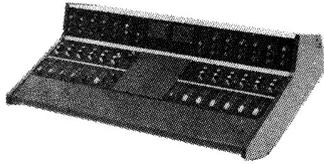
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TYPE	SERIES NO.	SEC. VOLTS	R.M.S. CURRENT
<b>18VA</b> Regulation 19% 62 x 34 (See diagram) 0.35 Kgs Mounting bolt M4 x 12	03010	6-6	1.25
	03011	9-9	0.83
	03012	12-12	0.63
	03013	15-15	0.50
	03014	18-18	0.42
	03015	22-22	0.34
	03016	25-25	0.30
<b>20VA</b> Regulation 18% Size A B C 70 35 37 0.45 Kgs Mounting bolt M5 x 50	13010	6-6	2.50
	13011	9-9	1.66
	13012	12-12	1.25
	13013	15-15	1.00
	13014	18-18	0.83
	13015	22-22	0.68
	13016	25-25	0.60
<b>30VA</b> Regulation 13% Size A B C 80 40 43 0.9 Kgs Mounting bolt M5 x 50	23010	6-6	4.16
	23011	9-9	2.77
	23012	12-12	2.08
	23013	15-15	1.66
	23014	18-18	1.38
	23015	22-22	1.13
	23016	25-25	1.00
<b>50VA</b> Regulation 12% Size A B C 95 40 43 1.0 Kgs Mounting bolt M5 x 50	33010	6-6	6.56
	33011	9-9	4.44
	33012	12-12	3.33
	33013	15-15	2.66
	33014	18-18	2.22
	33015	22-22	1.81
	33016	25-25	1.60
<b>120VA</b> Regulation 11% Size A B C 95 45 50 12 Kgs Mounting bolt M5 x 50	43010	6-6	10.00
	43011	9-9	6.66
	43012	12-12	5.00
	43013	15-15	4.00
	43014	18-18	3.33
	43015	22-22	2.72
	43016	25-25	2.40

TYPE	SERIES NO.	SEC. VOLTS	R.M.S. CURRENT
<b>100VA</b> Regulation 8% Size A B C 110 45 50 1.8 Kgs Mounting bolt M5 x 50	53011	9-9	8.89
	53012	12-12	6.66
	53013	15-15	5.33
	53014	18-18	4.44
	53015	22-22	3.63
	53016	25-25	3.20
	53017	30-30	2.66
	53018	35-35	2.28
	53026	40-40	2.00
	53028	110	1.45
	53029	220	0.72
<b>225VA</b> Regulation 7% Size A B C 110 50 55 2.2 Kgs Mounting bolt M5 x 60	63012	12-12	9.38
	63013	15-15	7.50
	63014	18-18	6.25
	63015	22-22	5.11
	63016	25-25	4.50
	63017	30-30	3.75
	63018	35-35	3.21
	63026	40-40	2.81
	63025	45-45	2.50
	63033	50-50	2.25
	63028	110	2.04
<b>300VA</b> Regulation 6% Size A B C 110 57 62 2.6 Kgs Mounting bolt M5 x 60	73013	15-15	10.00
	73014	18-18	8.33
	73015	22-22	6.82
	73016	25-25	6.00
	73017	30-30	5.00
	73018	35-35	4.28
	73026	40-40	3.75
	73025	45-45	3.33
	73033	50-50	3.00
	73028	110	2.72
	73029	220	1.36
<b>500VA</b> Regulation 5% Size A B C 135 60 65 4.0 Kgs Mounting bolt M8 x 70	83016	25-25	10.00
	83017	30-30	8.33
	83018	35-35	7.14
	83026	40-40	6.25
	83025	45-45	5.55
	83033	50-50	5.00
	83042	55-55	4.54
	83028	110	4.54
	83029	220	2.27
	83030	240	2.08

TYPE	SERIES NO.	SEC. VOLTS	R.M.S. CURRENT
<b>828VA</b> Regulation 4% Size A B C 140 70 75 5.0 Kgs Mounting bolt M8 x 90	93017	30-30	10.41
	93018	35-35	8.92
	93026	40-40	7.81
	93027	45-45	6.94
	93033	50-50	6.25
	93042	55-55	5.68
	93028	110	5.68
	93029	220	2.84
	93030	240	2.60

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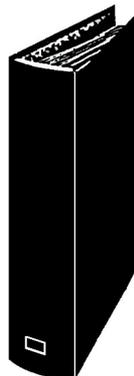
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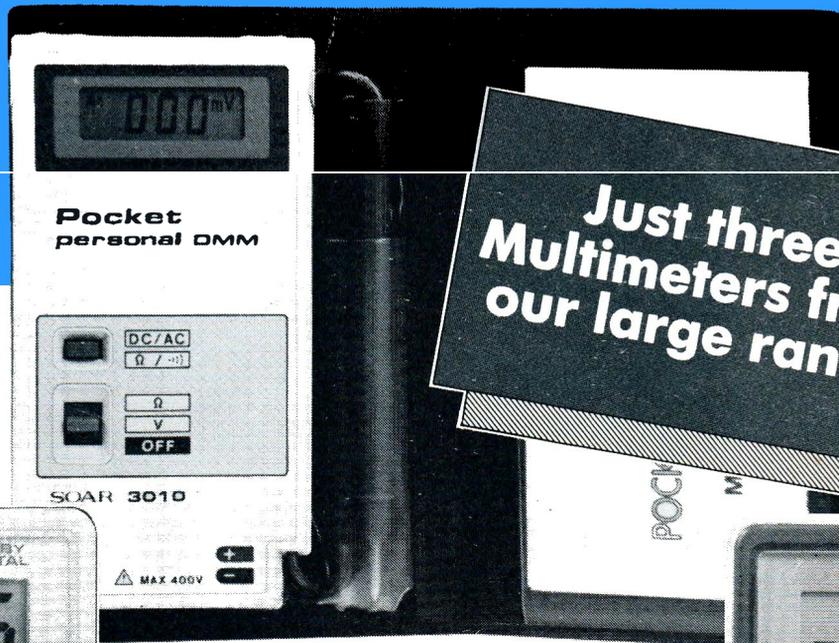
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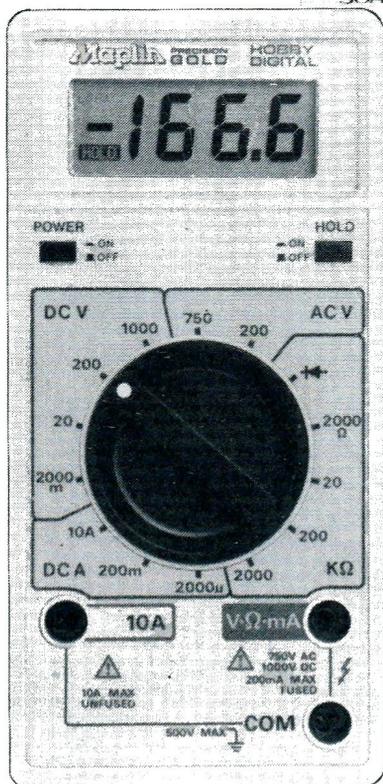
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